ABSTRACT
This application report provides basic circuits of the Texas Instruments op amp collection.

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1 Introduction

Texas Instruments recommends replacing 2N2920 and 2N3728 matched pairs with LM394 in all application circuits.

2 Basic Circuits

![Inverting Amplifier](image1)

\[ V_{OUT} = \frac{R_2}{R_1} V_{IN} \]
\[ R_N = R_1 \]

Figure 1. Inverting Amplifier

![Non-Inverting Amplifier](image2)

\[ V_{OUT} = \frac{R_1 + R_2}{R_1} V_{IN} \]

Figure 2. Non-Inverting Amplifier

![Difference Amplifier](image3)

\[ V_{OUT} = \left( \frac{R_1 + R_2}{R_3 + R_4} \right) \frac{R_2}{R_1} V_{1} - \frac{R_2}{R_1} V_{2} \]

For \( R_1 = R_3 \) and \( R_2 = R_4 \):
\[ V_{OUT} = \frac{R_2}{R_1} (V_2 - V_1) \]
\[ \frac{R_1}{R_2} = \frac{R_3}{R_4} \]

For minimum offset error due to input bias current.

Figure 3. Difference Amplifier
R5 = \( \frac{R1}{R2} \div \frac{R3}{R4} \)
For minimum offset error due to input bias current,

**Figure 4. Inverting Summing Amplifier**

* \( R_S = 1k \) for 1% accuracy

**Figure 5. Non-Inverting Summing Amplifier**

* Source impedance less than 100k gives less than 1% gain error.

**Figure 6. Inverting Amplifier with High Input Impedance**
**Figure 7. Fast Inverting Amplifier with High Input Impedance**

**Figure 8. Non-Inverting AC Amplifier**

\[
V_{OUT} = \frac{R1 + R2}{R1} V_{IN} \\
R_{IN} = R3 \\
R3 = \frac{R1}{R2}
\]
For minimum offset error due to input bias current.

Figure 9. Practical Differentiator

Figure 10. Integrator
**Figure 11. Fast Integrator**

\[ V_{\text{OUT}} = \frac{V_{\text{IN}}}{R_1} \]

*For minimum error due to bias current R2 = R1*

**Figure 12. Current to Voltage Converter**

\[ V_{\text{OUT}} = I_{\text{IN}} R_1 \]

*For minimum error due to bias current R2 = R1*
Figure 13. Circuit for Operating the LM101 Without a Negative Supply

Figure 14. Circuit for Generating the Second Positive Voltage

Figure 15. Neutralizing Input Capacitance to Optimize Response Time
* Adjust for zero integrator drift.
Current drift typically 0.1 nA/°C over −55°C to 125°C temperature range.

**Figure 16. Integrator with Bias Current Compensation**

**Figure 17. Voltage Comparator for Driving DTL or TTL Integrated Circuits**
Figure 18. Threshold Detector for Photodiodes

\[ V_{\text{OUT}} = 4.6V \text{ for } V_{\text{LT}} \leq V_{\text{IN}} \leq V_{\text{UT}} \]
\[ V_{\text{OUT}} = 0V \text{ for } V_{\text{IN}} < V_{\text{LT}} \text{ or } V_{\text{IN}} > V_{\text{UT}} \]

Figure 19. Double-Ended Limit Detector

\[ V_{\text{OUT}} = 4.6V \text{ for } V_{\text{LT}} \leq V_{\text{IN}} \leq V_{\text{UT}} \]
\[ V_{\text{OUT}} = 0V \text{ for } V_{\text{IN}} < V_{\text{LT}} \text{ or } V_{\text{IN}} > V_{\text{UT}} \]
Figure 20. Multiple Aperture Window Discriminator
Figure 21. Offset Voltage Adjustment for Inverting Amplifiers Using Any Type of Feedback Element

\[
\text{RANGE} = \pm V \left( \frac{R_2}{R_1} \right)
\]

Figure 22. Offset Voltage Adjustment for Non-Inverting Amplifiers Using Any Type of Feedback Element

\[
\text{RANGE} = \pm V \left( \frac{R_3}{R_1} \right)
\]
\[
\text{GAIN} = 1 + \frac{R_3}{R_4 + R_2}
\]

Figure 23. Offset Voltage Adjustment for Voltage Followers

\[
\text{RANGE} = \pm V \left( \frac{R_3}{R_1} \right)
\]
Figure 24. Offset Voltage Adjustment for Differential Amplifiers

Figure 25. Offset Voltage Adjustment for Inverting Amplifiers Using 10 kΩ Source Resistance or Less
### Figure 26. Low Frequency Sine Wave Generator with Quadrature Output

- **C2**: 0.02 \( \mu \)F, 1%
- **C1**: 0.01 \( \mu \)F, 1%
- **C4**: 30 pF
- **C3**: 0.01 \( \mu \)F, 1%
- **C5**: 30 pF
- **R1**: 22M, 1%
- **R2**: 22M, 1%
- **R3**: 10M, 1%
- **R4**: 50K
- **D1**: 6.3V
- **D2**: 6.3V

\[ f_0 = 1 \text{ Hz} \]
Figure 27. High Frequency Sine Wave Generator with Quadrature Output

* Chosen for oscillation at 100 Hz

Figure 28. Free-Running Multivibrator
Figure 29. Wein Bridge Sine Wave Oscillator

Figure 30. Function Generator

* Eldema 1869 10V, 14 mA Bulb

\[ f = \frac{1}{2\pi R_1 C_1} \]
Figure 31. Pulse Width Modulator

Figure 32. Bilateral Current Source

\[ I_{out} = \frac{R_3}{R_1 R_5} V_{IN} \]

\[ R_3 = R_4 + R_5 \]

\[ R_1 = R_2 \]
Figure 33. Bilateral Current Source

\[
\text{\( I_{\text{OUT}} \)} = \frac{R_3 \cdot V_{\text{IN}}}{R_1 \cdot R_5}
\]

\[
R_3 = R_4 + R_5
\]

\[
R_1 = R_2
\]
Figure 34. Wein Bridge Oscillator with FET Amplitude Stabilization
* $V_{\text{OUT}} = 1V/k\Omega$

Figure 35. Low Power Supply for Integrated Circuit Testing
Figure 36. Positive Voltage Reference

Figure 37. Positive Voltage Reference
Figure 38. Negative Voltage Reference

Figure 39. Negative Voltage Reference
Figure 40. Precision Current Sink

\[ I_O = \frac{V_{IN}}{R_1} \quad V_{IN} = 0V \]

Figure 41. Precision Current Source

\[ I_O = \frac{V_{IN}}{R_1} \quad V_{IN} \leq 0V \]

\[ I_O = \frac{V_{IN}}{R_2} \quad R_2 = 10K \]
Figure 42. Differential-Input Instrumentation Amplifier
* Gain adjust $A_v = 10^{-4} R_6$

Figure 43. Variable Gain, Differential-Input Instrumentation Amplifier
† Matching determines common mode rejection.

Figure 44. Instrumentation Amplifier with ±100 Volt Common Mode Range
Figure 45. Instrumentation Amplifier with ±10 Volt Common Mode Range
*† Matching Determines CMRR
‡ May be deleted to maximize bandwidth

**Figure 46. High Input Impedance Instrumentation Amplifier**

* Reduces feed through of power supply noise by 20 dB and makes supply bypassing unnecessary.
† Trim for best common mode rejection
‡ Gain adjust

**Figure 47. Bridge Amplifier with Low Noise Compensation**
Figure 48. Bridge Amplifier

\[ V_{OUT} = V^+ \left( 1 - \frac{R_1}{R_{S1}} \right) \]

Figure 49. Precision Diode
* \( E_{REF} \) must have a source impedance of less than 200Ω if D2 is used.

**Figure 50. Precision Clamp**

**Figure 51. Fast Half Wave Rectifier**
* Feedforward compensation can be used to make a fast full wave rectifier without a filter.

Figure 52. Precision AC to DC Converter

Figure 53. Low Drift Peak Detector
Figure 54. Absolute Value Amplifier with Polarity Detector

\[ V_{out} = -|V_{in}| \times \frac{R_2}{R_1} \]

\[ R_2 = \frac{R_4 + R_3}{R_3} \]
**Figure 55. Sample and Hold**

![Circuit Diagram 1](image1)

* Polycarbonate-dielectric capacitor

**Figure 56. Sample and Hold**

![Circuit Diagram 2](image2)

* Worst case drift less than 2.5 mV/sec
† Teflon, Polyethylene or Polycarbonate Dielectric Capacitor
Q1 and Q3 should not have internal gate-protection diodes. Worst case drift less than 500 μV/sec over −55°C to +125°C.

Figure 57. Low Drift Integrator
* In addition to increasing speed, the LM101A raises high and low frequency gain, increases output drive capability and eliminates thermal feedback.
† Power Bandwidth: 250 kHz
Small Signal Bandwidth: 3.5 MHz
Slew Rate: 10 V/μs

Figure 58. Fast† Summing Amplifier with Low Input Current
Figure 59. Fast Integrator with Low Input Current
Figure 60. Adjustable Q Notch Filter

\[ f_0 = \frac{1}{2\pi R_1 C_1} \]

- 60 Hz
- \( R_1 = R_2 = R_3 \)
- \( C_1 = C_2 = C_3 \)
Figure 61. Easily Tuned Notch Filter

$$f_0 = \frac{1}{2\pi R_4 C_1 C_2}$$

$$R_4 = R_5$$
$$R_1 = R_3$$
$$R_4 = \frac{1}{3} R_1$$

Figure 62. Tuned Circuit

$$f_0 = \frac{1}{2\pi R_1 R_2 C_1 C_2}$$
**Figure 63. Two-Stage Tuned Circuit**

\[ I_0 = \frac{1}{2 \pi R_1 R_2 C_1 C_2} \]

**Figure 64. Negative Capacitance Multiplier**

\[ C = \frac{R_2}{R_3} C_1 \]
\[ I_C = \frac{V_{os} + R_2 V_{os}}{R_3} \]
\[ R_S = \frac{R_3 (R_1 + R_{so})}{R_{so} A_{v0}} \]
Figure 65. Variable Capacitance Multiplier

\[ C = \left(1 + \frac{R_3}{R_2}\right)C_1 \]

Figure 66. Simulated Inductor

\[ L \geq R_1 R_2 C_1 \]
\[ R_2 = R_2 \]
\[ R_e = R_1 \]
Figure 67. Capacitance Multiplier

Figure 68. High Pass Active Filter

* Values are for 100 Hz cutoff. Use metalized polycarbonate capacitors for good temperature stability.
* Values are for 10 kHz cutoff. Use silvered mica capacitors for good temperature stability.

**Figure 69. Low Pass Active Filter**

**Figure 70. Nonlinear Operational Amplifier with Temperature Compensated Breakpoints**
Figure 71. Current Monitor

\[ V_{\text{out}} = \frac{R_1 R_3}{R_2} \]

Figure 72. Saturating Servo Preamplifier with Rate Feedback

\[ \text{LM103 } 2.4V \]

\[ \text{LM101A } \]

\[ \text{LM107 } \]

\[ \text{Q1} \]

\[ \text{R1} 0.1 \text{ } 1\% \]

\[ \text{R2} 100 \text{ } 1\% \]

\[ \text{R3} 5K \text{ } 1\% \]

\[ \text{D1} \]

\[ \text{D2} \]

\[ \text{C1} 50 \mu F \]

\[ \text{C2} 30 \text{ pF} \]

\[ \text{R2} 1.8K \]

\[ \text{R3} 100K \]
Figure 73. Power Booster

Figure 74. Analog Multiplier

\[ R_5 = R_1 \left( \frac{V_1}{10} \right) \]
\[ V_i \geq 0 \]
\[ V_{out} = \frac{V_1 V_2}{10} \]
* Low leakage $-0.017 \mu F$ per second delay

**Figure 75. Long Interval Timer**

Propagation delay approximately 200 ns
† DTL or TTL fanout of three.
Minimize stray capacitance
Pin 8

**Figure 76. Fast Zero Crossing Detector**
Low frequency cutoff = $R_1 \times C_1$

Figure 77. Amplifier for Piezoelectric Transducer

* Set for 0V at 0°C
† Adjust for 100 mV/°C

Figure 78. Temperature Probe
Figure 79. Photodiode Amplifier

\[ V_{\text{OUT}} = R_1 I_D \]

Figure 80. Photodiode Amplifier

\[ V_{\text{OUT}} = 10 \text{ V/\mu A} \]

*Operating photodiode with less than 3 mV across it eliminates leakage currents.

Figure 81. High Input Impedance AC Follower
10 nA < I_{IN} < 1 mA  
Sensitivity is 1V per decade  
† 1 kΩ (±1%) at 25°C, +3500 ppm/°C. 
Available from Vishay Ultronix, Grand Junction, CO, Q81 Series.  
* Determines current for zero crossing on output: 10 μA as shown.  

Figure 82. Temperature Compensated Logarithmic Converter  

*† 2N3728 matched pairs  

Figure 83. Root Extractor
Figure 84. Multiplier/Divider

Figure 85. Cube Generator
† 1 kΩ (±1%) at 25°C, +3500 ppm/°C.
Available from Vishay Ultronix, Grand Junction, CO, Q81 Series.

Figure 86. Fast Log Generator

† 1 kΩ (±1%) at 25°C, +3500 ppm/°C.
Available from Vishay Ultronix, Grand Junction, CO, Q81 Series.

Figure 87. Anti-Log Generator
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