1 Features

- Integrated Shielded Inductor
- Simple PCB Layout
- Frequency Synchronization Input (350 kHz to 600 kHz)
- Current Sharing Capability
- Flexible Startup Sequencing Using External Soft-start, Tracking and Precision Enable
- Protection Against Inrush Currents and Faults Such as Input UVLO and Output Short Circuit
- Junction Temperature Range –40°C to 125°C
- Single Exposed Pad and Standard Pinout for Easy Mounting and Manufacturing
- Fully Enabled for WEBENCH® Power Designer
- Pin Compatible With LMZ22010/08, LMZ12010/08, LMZ23608/06H, and LMZ13610/08/06H
- Performance Benefits
  - High Efficiency Reduces System Heat Generation
  - Low Radiated Emissions (EMI) Tested to EN55022 Class B Standard
  - Only 7 External Components
  - Low Output Voltage Ripple
  - No External Heat Sink Required
  - Simple Current Sharing for Higher Current Applications
- Electrical Specifications
  - 50-W Maximum Total Output Power
  - Up to 10-A Output Current
  - Input Voltage Range 6 V to 36 V
  - Output Voltage Range 0.8 V to 6 V
  - Efficiency up to 92%


2 Applications

- Point-of-load Conversions from 12-V and 24-V Input Rail
- Time-Critical Projects
- Space Constrained / High Thermal Requirement Applications
- Negative Output Voltage Applications (See AN-2027, SNVA425)

3 Description

The LMZ23610 SIMPLE SWITCHER® power module is an easy-to-use step-down DC-DC solution capable of driving up to 10-A load. The LMZ23610 is available in an innovative package that enhances thermal performance and allows for hand or machine soldering.

The LMZ23610 can accept an input voltage rail between 6 V and 36 V and can deliver an adjustable and highly accurate output voltage as low as 0.8 V. The LMZ23610 only requires two external resistors and three external capacitors to complete the power solution.

The LMZ23610 is a reliable and robust design with the following protection features: thermal shutdown, input undervoltage lockout, output overvoltage protection, short circuit protection, output current limit, and the device allows start-up into a prebiased output. The sync input allows synchronization over the 350- to 600-kHz switching frequency range.

Device Information

<table>
<thead>
<tr>
<th>PART NUMBER</th>
<th>PACKAGE</th>
<th>BODY SIZE (NOM)</th>
</tr>
</thead>
<tbody>
<tr>
<td>LMZ23610</td>
<td>NDY (11)</td>
<td>15.00 mm × 15.00 mm</td>
</tr>
</tbody>
</table>

(1) For all available packages, see the orderable addendum at the end of the data sheet.

(2) Peak reflow temperature equals 245°C. See SNA214 for more details.

Simplified Application Schematic

Efficiency 3.3-V Output at 25°C
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# 4 Revision History

NOTE: Page numbers for previous revisions may differ from page numbers in the current version.

Changes from Revision F (August 2015) to Revision G Page

• Changed this pin table to match the pin out diagram ........................................ 3

Changes from Revision E (October 2013) to Revision F Page

• Removed Easy-To-Use PFM 7-Pin Package image ........................................ 1
• Added Pin Configuration and Functions section, ESD Ratings table, Feature Description section, Device Functional Modes, Application and Implementation section, Power Supply Recommendations section, Layout section, Device and Documentation Support section, and Mechanical, Packaging, and Orderable Information section .......................... 1

Changes from Revision D (December 2012) to Revision E Page

• Deleted 12 mil .......................................................................... 4
• Changed 12 mil ......................................................................... 28
• Added Power Module SMT Guidelines........................................ 28
## Pin Configuration and Functions

### Pin Functions

<table>
<thead>
<tr>
<th>PIN</th>
<th>TYPE</th>
<th>DESCRIPTION</th>
</tr>
</thead>
<tbody>
<tr>
<td>NAME</td>
<td>NO.</td>
<td></td>
</tr>
<tr>
<td>VIN</td>
<td>1, 2</td>
<td>Power</td>
</tr>
<tr>
<td>SYNC</td>
<td>3</td>
<td>Analog</td>
</tr>
<tr>
<td>EN</td>
<td>4</td>
<td>Analog</td>
</tr>
<tr>
<td>AGND</td>
<td>5, 6</td>
<td>Ground</td>
</tr>
<tr>
<td>FB</td>
<td>7</td>
<td>Analog</td>
</tr>
<tr>
<td>SS</td>
<td>8</td>
<td>Analog</td>
</tr>
<tr>
<td>SH</td>
<td>9</td>
<td>Analog</td>
</tr>
<tr>
<td>VOUT</td>
<td>10, 11</td>
<td>Power</td>
</tr>
<tr>
<td>PGND</td>
<td>EP</td>
<td>Ground</td>
</tr>
</tbody>
</table>
6 Specifications

6.1 Absolute Maximum Ratings
over operating free-air temperature range (unless otherwise noted) (1)(2)

<table>
<thead>
<tr>
<th>Parameter</th>
<th>MIN</th>
<th>MAX</th>
<th>UNIT</th>
</tr>
</thead>
<tbody>
<tr>
<td>VIN to PGND</td>
<td>−0.3</td>
<td>40</td>
<td>V</td>
</tr>
<tr>
<td>EN, SYNC to AGND</td>
<td>−0.3</td>
<td>5.5</td>
<td>V</td>
</tr>
<tr>
<td>SS, FB, SH to AGND</td>
<td>−0.3</td>
<td>2.5</td>
<td>V</td>
</tr>
<tr>
<td>AGND to PGND</td>
<td>−0.3</td>
<td>0.3</td>
<td>V</td>
</tr>
<tr>
<td>Junction temperature</td>
<td>150°C</td>
<td></td>
<td></td>
</tr>
<tr>
<td>Storage temperature, T_{stg}</td>
<td>−65</td>
<td>150</td>
<td>°C</td>
</tr>
</tbody>
</table>

(1) Stresses beyond those listed under Absolute Maximum Ratings may cause permanent damage to the device. These are stress ratings only, which do not imply functional operation of the device at these or any other conditions beyond those indicated under Recommended Operating Conditions. Exposure to absolute-maximum-rated conditions for extended periods may affect device reliability.

(2) For soldering specifications: see product folder at www.ti.com and ISNOA549

6.2 ESD Ratings

<table>
<thead>
<tr>
<th>Parameter</th>
<th>VALUE</th>
<th>UNIT</th>
</tr>
</thead>
<tbody>
<tr>
<td>V_{(ESD)} Electrostatic discharge</td>
<td>Human body model (HBM), per ANSI/ESDA/JEDEC JS-001(1)</td>
<td>±2000 V</td>
</tr>
</tbody>
</table>

(1) JEDEC document JEP155 states that 500-V HBM allows safe manufacturing with a standard ESD control process.

6.3 Recommended Operating Conditions
over operating free-air temperature range (unless otherwise noted)

<table>
<thead>
<tr>
<th>Parameter</th>
<th>MIN</th>
<th>MAX</th>
<th>UNIT</th>
</tr>
</thead>
<tbody>
<tr>
<td>VIN</td>
<td>6</td>
<td>36</td>
<td>V</td>
</tr>
<tr>
<td>EN, SYNC</td>
<td>0</td>
<td>5</td>
<td>V</td>
</tr>
<tr>
<td>Operation Junction Temperature</td>
<td>−40</td>
<td>125</td>
<td>°C</td>
</tr>
</tbody>
</table>

6.4 Thermal Information

<table>
<thead>
<tr>
<th>THERMAL METRIC(1)</th>
<th>LMZ23610</th>
<th>UNIT</th>
</tr>
</thead>
<tbody>
<tr>
<td>R_{JUA} Junction-to-ambient thermal resistance(2)</td>
<td>11 PINS</td>
<td>°C/W</td>
</tr>
<tr>
<td>Natural Convection</td>
<td>9.9</td>
<td></td>
</tr>
<tr>
<td>225 LFPM</td>
<td>6.8</td>
<td></td>
</tr>
<tr>
<td>500 LFPM</td>
<td>5.2</td>
<td></td>
</tr>
<tr>
<td>R_{JUC(top)} Junction-to-case (top) thermal resistance</td>
<td>1.0 °C/W</td>
<td></td>
</tr>
</tbody>
</table>

(1) For more information about traditional and new thermal metrics, see the Semiconductor and IC Package Thermal Metrics application report, SPRA953.

(2) R_{JUA} measured on a 3.0-in × 3.5-in 4-layer board, with 2-oz. copper on outer layers and 1-oz. copper on inner layers, two hundred and ten thermal vias, and 2-W power dissipation. Refer to evaluation board application note layout diagrams.
6.5 Electrical Characteristics

Limits are for \( T_J = 25°C \) unless otherwise specified. Minimum and Maximum limits are specified through test, design or statistical correlation. Typical values represent the most likely parametric norm at \( T_J = 25°C \), and are provided for reference purposes only. Unless otherwise stated the following conditions apply: \( V_{IN} = 12V, V_{OUT} = 3.3V \)

<table>
<thead>
<tr>
<th>PARAMETER</th>
<th>TEST CONDITIONS</th>
<th>MIN(1)</th>
<th>TYP(2)</th>
<th>MAX(1)</th>
<th>UNIT</th>
</tr>
</thead>
<tbody>
<tr>
<td><em><strong>SYSTEM PARAMETERS</strong></em></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>( V_{EN} )</td>
<td>EN threshold</td>
<td>( V_{EN} ) rising over the junction temperature ( (T_J) ) range of (-40°C ) to ( +125°C )</td>
<td>1.274</td>
<td></td>
<td>V</td>
</tr>
<tr>
<td>( I_{EN-HYS} )</td>
<td>EN hysteresis source current</td>
<td>( V_{EN} &gt; 1.274 ) V</td>
<td></td>
<td>13</td>
<td>( \mu )A</td>
</tr>
<tr>
<td><em><strong>SOFTWARE</strong></em></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>( I_{SS} )</td>
<td>SS source current</td>
<td>( V_{SS} = 0 ) V over the junction temperature ( (T_J) ) range of (-40°C ) to ( +125°C )</td>
<td>50</td>
<td></td>
<td>( \mu )A</td>
</tr>
<tr>
<td>( I_{SS} )</td>
<td>Internal soft-start interval</td>
<td></td>
<td>1.6</td>
<td></td>
<td>ms</td>
</tr>
<tr>
<td><em><strong>CURRENT LIMIT</strong></em></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>( I_{CL} )</td>
<td>Current limit threshold</td>
<td>DC average</td>
<td>12.5</td>
<td></td>
<td>A</td>
</tr>
<tr>
<td><em><strong>INTERNAL SWITCHING OSCILLATOR</strong></em></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>( f_{osc} )</td>
<td>Free-running oscillator frequency</td>
<td>Sync input connected to ground</td>
<td>314</td>
<td>359</td>
<td>404</td>
</tr>
<tr>
<td>( f_{sync} )</td>
<td>Synchronization range</td>
<td>( V_{sync} = 3.3 ) Vp-p</td>
<td>314</td>
<td>600</td>
<td>kHz</td>
</tr>
<tr>
<td>( V_L_{sync} )</td>
<td>Synchronization logic zero amplitude</td>
<td>Relative to AGND over the junction temperature ( (T_J) ) range of (-40°C ) to ( +125°C )</td>
<td>0.4</td>
<td></td>
<td>V</td>
</tr>
<tr>
<td>( V_H_{sync} )</td>
<td>Synchronization logic one amplitude</td>
<td>Relative to AGND over the junction temperature ( (T_J) ) range of (-40°C ) to ( +125°C )</td>
<td>1.8</td>
<td></td>
<td>V</td>
</tr>
<tr>
<td>( \text{Sync}_{%} )</td>
<td>Synchronization duty cycle range</td>
<td></td>
<td>15%</td>
<td>50%</td>
<td>85%</td>
</tr>
<tr>
<td><em><strong>REGULATION AND OVERTOLTAGE COMPARATOR</strong></em></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>( V_{FB} )</td>
<td>In-regulation feedback voltage</td>
<td>( V_{SS} \rightarrow 0.8 ) V ( I_D = 10 ) A over the junction temperature ( (T_J) ) range of (-40°C ) to ( +125°C )</td>
<td>0.795</td>
<td></td>
<td>V</td>
</tr>
<tr>
<td>( V_{FB-OV} )</td>
<td>Feedback over-voltage protection threshold</td>
<td></td>
<td>0.86</td>
<td></td>
<td>V</td>
</tr>
<tr>
<td>( I_{FB} )</td>
<td>Feedback input bias current</td>
<td></td>
<td>5</td>
<td></td>
<td>nA</td>
</tr>
<tr>
<td>( I_Q )</td>
<td>Non-switching quiescent current</td>
<td>SYNC = 3.0 V</td>
<td>3</td>
<td></td>
<td>mA</td>
</tr>
<tr>
<td>( I_{SD} )</td>
<td>Shutdown quiescent current</td>
<td>( V_{EN} = 0 ) V</td>
<td>32</td>
<td></td>
<td>( \mu )A</td>
</tr>
<tr>
<td>( D_{MAX} )</td>
<td>Maximum duty factor</td>
<td></td>
<td>85%</td>
<td></td>
<td></td>
</tr>
<tr>
<td><em><strong>THERMAL CHARACTERISTICS</strong></em></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>( T_{SD} )</td>
<td>Thermal shutdown Rising</td>
<td></td>
<td>165</td>
<td></td>
<td>°C</td>
</tr>
<tr>
<td>( T_{SD-HYST} )</td>
<td>Thermal shutdown hysteresis Falling</td>
<td></td>
<td>15</td>
<td></td>
<td>°C</td>
</tr>
<tr>
<td><em><strong>PERFORMANCE PARAMETERS</strong></em>(3)</td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>( \Delta V_{O} )</td>
<td>Output voltage ripple BW at 20 MHz</td>
<td></td>
<td>24</td>
<td></td>
<td>mVpp</td>
</tr>
<tr>
<td>( \Delta V_{O}/V_{IN} )</td>
<td>Line regulation ( V_{IN} = 12 ) V to 20 V, ( I_{OUT} = 10 ) A</td>
<td></td>
<td>( \pm 0.2% )</td>
<td></td>
<td></td>
</tr>
<tr>
<td>( \Delta V_{O}/I_{OUT} )</td>
<td>Load regulation ( V_{IN} = 12 ) V, ( I_{OUT} = 0.001 ) A to 10 A</td>
<td></td>
<td>1</td>
<td></td>
<td>mV/A</td>
</tr>
<tr>
<td>( \eta )</td>
<td>Peak efficiency ( V_{IN} = 12 ) V, ( V_{OUT} = 3.3 ) V, ( I_{OUT} = 5 ) A</td>
<td></td>
<td>89.5%</td>
<td></td>
<td></td>
</tr>
<tr>
<td>( \eta )</td>
<td>Full load efficiency ( V_{IN} = 12 ) V, ( V_{OUT} = 3.3 ) V, ( I_{OUT} = 10 ) A</td>
<td></td>
<td>87.5%</td>
<td></td>
<td></td>
</tr>
</tbody>
</table>

(1) Minimum and Maximum limits are 100% production tested at 25°C. Limits over the operating temperature range are specified through correlation using Statistical Quality Control (SQC) methods. Limits are used to calculate TI’s Average Outgoing Quality Level (AOQL).
(2) Typical numbers are at 25°C and represent the most likely parametric norm.
(3) Refer to BOM in Table 1.
6.6 Typical Characteristics
Unless otherwise specified, the following conditions apply: \( V_{IN} = 12 \text{ V} \); \( C_{IN} = \text{three } \times \, 10 \mu\text{F} + 47-nF \text{ X7R Ceramic} \); \( C_{OUT} = \text{two } \times \, 330-\mu\text{F Specialty Polymer} + 47-\mu\text{F Ceramic} + 47-nF \text{ Ceramic} \); \( C_{FF} = 4.7 \text{ nF} \); \( T_A = 25^\circ \text{ C} \) for waveforms. All indicated temperatures are ambient.

Figure 1. Efficiency 5-V Output at 25°C
Figure 2. Dissipation 5-V Output at 25°C
Figure 3. Efficiency 3.3-V Output at 25°C
Figure 4. Dissipation 3.3-V Output at 25°C
Figure 5. Efficiency 2.5-V Output at 25°C
Figure 6. Dissipation 2.5-V Output at 25°C
Typical Characteristics (continued)

Unless otherwise specified, the following conditions apply: $V_{IN} = 12\, \text{V}$; $C_{IN} = \text{three} \times 10\, \mu\text{F} + 47\, \text{nF} \times 7\text{R Ceramic}$; $C_{OUT} = \text{two} \times 330\, \mu\text{F} \times \text{Specialty Polymer} + 47\, \mu\text{F Ceramic} + 47\, \text{nF Ceramic}$; $C_{FF} = 4.7\, \text{nF}$; $T_A = 25^\circ\, \text{C}$ for waveforms. All indicated temperatures are ambient.

Figure 7. Efficiency 1.8-V Output at 25°C

Figure 8. Dissipation 1.8-V Output at 25°C

Figure 9. Efficiency 1.5-V Output at 25°C

Figure 10. Dissipation 1.5-V Output at 25°C

Figure 11. Efficiency 1.2-V Output at 25°C

Figure 12. Dissipation 1.2-V Output at 25°C
Typical Characteristics (continued)

Unless otherwise specified, the following conditions apply: $V_{IN} = 12$ V; $C_{IN} =$ three $\times$ 10 µF + 47-nF X7R Ceramic; $C_{OUT} =$ two $\times$ 330-µF Specialty Polymer + 47-µF Ceramic + 47-nF Ceramic; $C_{FF} = 4.7$ nF; $T_A = 25^\circ$ C for waveforms. All indicated temperatures are ambient.
Typical Characteristics (continued)

Unless otherwise specified, the following conditions apply: \( V_{IN} = 12 \, V \); \( C_{IN} = \text{three} \times 10 \, \mu F + 47 \, nF \, X7R \, \text{Ceramic} \); \( C_{OUT} = \text{two} \times 330 \, \mu F \, \text{Specialty Polymer} + 47 \, \mu F \, \text{Ceramic} + 47 \, nF \, \text{Ceramic} \); \( C_{FF} = 4.7 \, nF \); \( T_A = 25^\circ \, C \) for waveforms. All indicated temperatures are ambient.

Figure 19. Efficiency 2.5-V Output at 85°C

Figure 20. Dissipation 2.5-V Output at 85°C

Figure 21. Efficiency 1.8-V Output at 85°C

Figure 22. Dissipation 1.8-V Output at 85°C

Figure 23. Efficiency 1.5-V Output at 85°C

Figure 24. Dissipation 1.5-V Output at 85°C
Typical Characteristics (continued)

Unless otherwise specified, the following conditions apply: $V_{IN} = 12$ V; $C_{IN} = 3 \times 10 \mu F + 47$-nF X7R Ceramic; $C_{OUT} = 2 \times 330$-$\mu F$ Specialty Polymer + $47$-$\mu F$ Ceramic + $47$-nF Ceramic; $C_{FF} = 4.7$ nF; $T_A = 25^\circ C$ for waveforms. All indicated temperatures are ambient.

---

**Figure 25. Efficiency 1.2-V Output at 85°C**

**Figure 26. Dissipation 1.2-V Output at 85°C**

**Figure 27. Efficiency 1-V Output at 85°C**

**Figure 28. Dissipation 1-V Output at 85°C**

**Figure 29. Normalized Line and Load Regulation**

$V_{OUT} = 3.3$ V

**Figure 30. Thermal Derating**

$V_{IN} = 24$ V, $V_{OUT} = 5$ V
Typical Characteristics (continued)

Unless otherwise specified, the following conditions apply: \( V_{\text{IN}} = 12 \, \text{V} \); \( C_{\text{IN}} \) = three \( \times 10 \, \mu\text{F} \) + 47-nF X7R Ceramic; \( C_{\text{OUT}} \) = two \( \times 330-\mu\text{F} \) Specialty Polymer + 47-\( \mu\text{F} \) Ceramic + 47-nF Ceramic; \( C_{\text{FF}} \) = 4.7 nF; \( T_A = 25^\circ \text{C} \) for waveforms. All indicated temperatures are ambient.

\[ V_{\text{IN}} = 24 \, \text{V}, \quad V_{\text{OUT}} = 3.3 \, \text{V} \]

**Figure 31. Thermal Derating**

**Figure 32. \( R_{\text{thJA}} \) vs Copper Heat Sinking Area**

**Figure 33. Output Ripple**

12 \( V_{\text{IN}} \), 5 \( V_{\text{OUT}} \) at Full Load, BW = 20 MHz

**Figure 34. Output Ripple**

12 \( V_{\text{IN}} \), 5 \( V_{\text{OUT}} \) at Full Load, BW = 250 MHz

**Figure 35. Output Ripple**

12 \( V_{\text{IN}} \), 3.3 \( V_{\text{OUT}} \) at Full Load, BW = 20 MHz

**Figure 36. Output Ripple**

12 \( V_{\text{IN}} \), 3.3 \( V_{\text{OUT}} \) at Full Load, BW = 250 MHz
Typical Characteristics (continued)

Unless otherwise specified, the following conditions apply: $V_{IN} = 12$ V; $C_{IN} =$ three $\times$ 10 µF + 47-nF X7R Ceramic; $C_{OUT} =$ two $\times$ 330-µF Specialty Polymer + 47-µF Ceramic + 47-nF Ceramic; $C_{FF} =$ 4.7 nF; $T_A =$ 25° C for waveforms. All indicated temperatures are ambient.

![Figure 37. Output Ripple](image)

12 $V_{IN}$, 1.2 $V_{OUT}$ at Full Load, BW = 20 MHz

![TIME (2 µs/Div)](image)

![Figure 38. Output Ripple](image)

12 $V_{IN}$, 1.2 $V_{OUT}$ at Full Load, BW = 250 MHz

![TIME (2 µs/Div)](image)

![Figure 39. Transient Response](image)

12 $V_{IN}$, 5 $V_{OUT}$, 1- to 10-A Step

![TIME (500 µs/Div)](image)

![Figure 40. Transient Response](image)

12 $V_{IN}$, 3.3 $V_{OUT}$, 1- to 10-A Step

![TIME (500 µs/Div)](image)

![Figure 41. Transient Response](image)

12 $V_{IN}$, 1.2 $V_{OUT}$, 1- to 10-A Step

![TIME (500 µs/Div)](image)

![Figure 42. Short Circuit Current vs Input Voltage](image)

![CURRENT (A)](image)

5 10 15 20

0

2

4

6

8

10

12

14

16

INPUT VOLTAGE (V)

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Product Folder Links: LMZ23610
Typical Characteristics (continued)

Unless otherwise specified, the following conditions apply: \( V_{IN} = 12 \text{ V} \); \( C_{IN} = \text{three } \times 10 \mu \text{F } + 47\text{-nF X7R Ceramic; } C_{OUT} = \text{two } x 330\mu \text{F Specialty Polymer } + 47\mu \text{F Ceramic } + 47\text{-nF Ceramic; } C_{FF} = 4.7 \text{ nF; } T_A = 25^\circ \text{C for waveforms. All indicated temperatures are ambient.} \)

![Waveform Diagram](image)

**Figure 43. 3.3 \( V_{OUT} \) Soft-Start**

**Figure 44. 3.3 \( V_{OUT} \) Soft-Start**
7 Detailed Description

7.1 Overview
The architecture used is an internally compensated emulated peak current mode control, based on a monolithic synchronous SIMPLE SWITCHER core capable of supporting high load currents. The output voltage is maintained through feedback compared with an internal 0.8-V reference. For emulated peak current-mode, the valley current is sampled on the down-slope of the inductor current. This is used as the DC value of current to start the next cycle.

The primary application for emulated peak current-mode is high input voltage to low output voltage operating at a narrow duty cycle. By sampling the inductor current at the end of the switching cycle and adding an external ramp, the minimum ON-time can be significantly reduced, without the need for blanking or filtering which is normally required for peak current-mode control.

7.2 Functional Block Diagram

7.3 Feature Description
7.3.1 Synchronization Input
The PWM switching frequency can be synchronized to an external frequency source. The PWM switching will be in phase with the external frequency source. If this feature is not used, connect this input either directly to ground, or connect to ground through a resistor of 1.5 kΩ or less. The allowed synchronization frequency range is 314 kHz to 600 kHz. The typical input threshold is 1.4 V. Ideally, the input clock must overdrive the threshold by a factor of 2, so direct drive from 3.3-V logic through a 1.5-kΩ or less Thevenin source resistance is recommended. Note that applying a sustained logic 1 corresponds to 0-Hz PWM frequency and will cause the module to stop switching.

7.3.2 Current Sharing
When a load current higher than 10 A is required by the application, the LMZ23610 can be configured to share the load between multiple devices. To share the load current between the devices, connect the SH pin of all current sharing LMZ23610 modules. One device must be configured as the master by connecting FB normally. All other devices must be configured as slaves by leaving their respective FB pins floating. The modules must be synchronized by a clock signal to avoid beat frequencies in the output voltage caused by small differences in the internal 359-kHz clock. If the modules are not synchronized, the magnitude of the ripple voltage will depend on the phase relationship of the internal clocks. The external synchronizing clocks can be in phase for all modules,
Feature Description (continued)

or out of phase to reduce the current stress on the input and output capacitors. As an example, two modules can be run 180 degrees out of phase, and three modules can be run 120 degrees out of phase. The VIN, VOUT, PGND, and AGND pins must also be connected with low impedance paths. It is particularly important to pay close attention to the layout of AGND and SH, as offsets in grounding or noise picked up from other devices will be seen as a mismatch in current sharing and could cause noise issues.

Current sharing modules can be configured to share the same set of bulk input and output capacitors, while each having their own local input and output bypass capacitors. A \( C_{\text{IN\_BYP}} \geq 30 \ \mu\text{F} \) is still recommended for each module that is connected in a current sharing configuration. A \( C_{\text{OUT\_BYP}} \) consisting of 47-nF X7R ceramic capacitor in parallel with a 22-\( \mu\)F ceramic capacitor is recommended to locally bypass the output voltage for each module. These capacitors will provide local bypassing of high-frequency switched currents.

In a current sharing system using two or more modules, the slaves have their error amp circuitry disconnected. The master overrides the error amplifier outputs of the slaves. This signal is then compared to each module’s individual current sense circuitry. Due to this, the current sense gain of the entire system increases according to the number of modules slaved to the master. To compensate for this and ensure good stability, the total output capacitance has to be increased. For example, two modules configured to provide 1.2 V \( \text{OUT} \) and 20 amps have a required total bulk output capacitance of \( C_{\text{OUT\_BULK}} = 2 \times 450-\mu\text{F (ESR 25 m}\Omega) \). This is a thirty six percent increase in the required output capacitance of a stand alone module. Up to 6 modules can be connected in parallel for loads up to 60 A. For more information on current sharing refer to AN-2093 (SNVA460).

![Figure 45. Current Sharing Example Schematic](image-url)
Feature Description (continued)

![Figure 46. Output Voltage Ripple of Two Modules With Synchronization Clocks in Phase](image)

7.3.3 Output Overvoltage Protection

If the voltage at FB is greater than a 0.86-V internal reference, the output of the error amplifier is pulled toward ground, causing $V_{OUT}$ to fall.

7.3.4 Current Limit

The LMZ23610 is protected by both low-side (LS) and high-side (HS) current limit circuitry. The LS current limit detection is carried out during the OFF-time by monitoring the current through the LS synchronous MOSFET. Referring to the [Functional Block Diagram](functional_block_diagram), when the top MOSFET is turned off, the inductor current flows through the load, the PGND pin and the internal synchronous MOSFET. If this current exceeds 13 A (typical), the current limit comparator disables the start of the next switching period. Switching cycles are prohibited until current drops below the limit.

**NOTE**

DC current limit is dependent on duty cycle as illustrated in the graph in the *Typical Characteristics* section.

The HS current limit monitors the current of the top side MOSFET. Once HS current limit is detected (16 A typical), the HS MOSFET is shut off immediately, until the next cycle. Exceeding HS current limit causes $V_{OUT}$ to fall. Typical behavior of exceeding LS current limit is that $f_{SW}$ drops to 1/2 of the operating frequency.

7.3.5 Thermal Protection

The junction temperature of the LMZ23610 must not be allowed to exceed its maximum ratings. Thermal protection is implemented by an internal Thermal Shutdown circuit which activates at 165°C (typical) causing the device to enter a low power standby state. In this state the main MOSFET remains off causing $V_{OUT}$ to fall, and additionally the $C_{SS}$ capacitor is discharged to ground. Thermal protection helps prevent catastrophic failures for accidental device overheating. When the junction temperature falls back below 150 °C (typical hysteresis = 15°C) the SS pin is released, $V_{OUT}$ rises smoothly, and normal operation resumes.

Applications requiring maximum output current especially those at high input voltage may require additional derating at elevated temperatures.

7.3.6 Prebiased Start-Up

The LMZ23610 will properly start up into a prebiased output. This start-up situation is common in multiple rail logic applications where current paths may exist between different power rails during the start-up sequence. The following scope capture shows proper behavior in this mode. Trace one is Enable going high. Trace two is 1.8-V prebias rising to 3.3 V. Trace three is the SS voltage with a $C_{SS} = 0.47 \mu F$. Rise-time determined by $C_{SS}$. 
Feature Description (continued)

Figure 48. Prebiased Start-Up

7.3.6.1 Tracking Supply Divider Option

The tracking function allows the module to be connected as a slave supply to a primary voltage rail (often the 3.3-V system rail) where the slave module output voltage is lower than that of the master. Proper configuration allows the slave rail to power up coincident with the master rail such that the voltage difference between the rails during ramp-up is small (that is, < 0.15 V typical). The values for the tracking resistive divider must be selected such that the effect of the internal 50-µA current source is minimized. In most cases the ratio of the tracking divider resistors is the same as the ratio of the output voltage setting divider. Proper operation in tracking mode dictates the soft-start time of the slave rail be shorter than the master rail; a condition that is easy to satisfy because the \( C_{SS} \) cap is replaced by \( R_{TKB} \). The tracking function is only supported for the power up interval of the master supply; once the SS/TRK rises past 0.795 V the input is no longer enabled and the 50-µA internal current source is switched off.

Figure 49. Tracking Option Input Detail

7.4 Device Functional Modes

7.4.1 Discontinuous Conduction and Continuous Conduction Modes

At light load the regulator will operate in discontinuous conduction mode (DCM). With load currents above the critical conduction point, it will operate in continuous conduction mode (CCM). When operating in DCM, inductor current is maintained to an average value equaling \( I_{OUT} \). In DCM the low-side switch will turn off when the inductor current falls to zero, this causes the inductor current to resonate. Although it is in DCM, the current is allowed to go slightly negative to charge the bootstrap capacitor.

In CCM, current flows through the inductor through the entire switching cycle and never falls to zero during the OFF-time.
Device Functional Modes (continued)

Figure 50 is a comparison pair of waveforms showing both the CCM (upper) and DCM operating modes.

\[ V_{\text{IN}} = 12 \text{ V}, \quad V_{\text{O}} = 3.3 \text{ V}, \quad I_{\text{O}} = 3 \text{ A} / 0.3 \text{ A} \]

**Figure 50. CCM and DCM Operating Modes**
8 Application and Implementation

NOTE
Information in the following applications sections is not part of the TI component specification, and TI does not warrant its accuracy or completeness. TI’s customers are responsible for determining suitability of components for their purposes. Customers should validate and test their design implementation to confirm system functionality.

8.1 Application Information
The LMZ23610 is a step-down DC-to-DC power module. It is typically used to convert a higher DC voltage to a lower DC voltage with a maximum output current of 10 A. The following design procedure can be used to select components for the LMZ23610. Alternately, the WEBENCH software may be used to generate complete designs.

When generating a design, the WEBENCH software uses iterative design procedure and accesses comprehensive databases of components. Please go to www.ti.com for more details.

8.2 Typical Application

8.2.1 Design Requirements
For this example the following application parameters exist:
- \( V_{IN} \) Range = Up to 36 V
- \( V_{OUT} \) = 0.8 V to 6 V
- \( I_{OUT} \) = 10 A

8.2.2 Detailed Design Procedure

8.2.2.1 Design Steps
The LMZ23610 is fully supported by WEBENCH which offers: component selection, electrical and thermal simulations. Additionally, there are both evaluation and demonstration boards that may be used as a starting point for design. The following list of steps can be used to manually design the LMZ23610 application.

All references to values refer to the Figure 51.

1. Select minimum operating \( V_{IN} \) with enable divider resistors
2. Program \( V_{OUT} \) with FB resistor divider selection
3. Select \( C_{OUT} \)
4. Select \( C_{IN} \)
5. Determine module power dissipation
Typical Application (continued)

6. Layout PCB for required thermal performance

8.2.2.2 Enable Divider, \( R_{\text{ENT}}, R_{\text{ENB}} \) and \( R_{\text{ENH}} \) Selection

Internal to the module is a 2-MΩ pullup resistor connected from \( V_{\text{IN}} \) to Enable. For applications not requiring precision undervoltage lockout (UVLO), the Enable input may be left open circuit and the internal resistor will always enable the module. In such case, the internal UVLO occurs typically at 4.3 V (\( V_{\text{IN}} \) rising).

In applications with separate supervisory circuits Enable can be directly interfaced to a logic source. In the case of sequencing supplies, the divider is connected to a rail that becomes active earlier in the power-up cycle than the LMZ23610 output rail.

Enable provides a precise 1.274-V threshold to allow direct logic drive or connection to a voltage divider from a higher enable voltage such as \( V_{\text{IN}} \). Additionally there is 13 µA (typical) of switched offset current allowing programmable hysteresis. See Figure 52.

The function of the enable divider is to allow the designer to choose an input voltage below which the circuit will be disabled. This implements the feature of a programmable UVLO. The two resistors must be chosen based on the following ratio:

\[
\frac{R_{\text{ENT}}}{R_{\text{ENB}}} = \frac{V_{\text{IN UVLO}}}{1.274 \text{ V}} - 1
\]

The LMZ23610 typical application shows 12.7 kΩ for \( R_{\text{ENB}} \) and 42.2 kΩ for \( R_{\text{ENT}} \) resulting in a rising UVLO of 5.51 V. Note that this divider presents 4.62 V to the EN input when \( V_{\text{IN}} \) is raised to 20 V. This upper voltage must always be checked, making sure that it never exceeds the Abs Max 5.5-V limit for Enable. A 5.1-V Zener clamp can be applied in cases where the upper voltage would exceed the EN input's range of operation. The Zener clamp is not required if the target application prohibits the maximum Enable input voltage from being exceeded.

Additional enable voltage hysteresis can be added with the inclusion of \( R_{\text{ENH}} \). It is possible to select values for \( R_{\text{ENT}} \) and \( R_{\text{ENB}} \) such that \( R_{\text{ENH}} \) is a value of zero allowing it to be omitted from the design.

Rising threshold can be calculated as follows:

\[
V_{\text{EN}}(\text{rising}) = 1.274 \left( 1 + \frac{R_{\text{ENT}} || 2 \text{ meg}}{R_{\text{ENB}}} \right)
\]

Whereas the falling threshold level can be calculated using:

\[
V_{\text{EN}}(\text{falling}) = V_{\text{EN}}(\text{rising}) - 13 \mu\text{A} \left( R_{\text{ENT}} || 2 \text{ meg} || R_{\text{ENB}} + R_{\text{ENH}} \right)
\]

8.2.2.3 Output Voltage Selection

Output voltage is determined by a divider of two resistors connected between \( V_{\text{OUT}} \) and AGND. The midpoint of the divider is connected to the FB input.

The regulated output voltage determined by the external divider resistors \( R_{\text{FBT}} \) and \( R_{\text{FBB}} \) is:
Typical Application (continued)

\[ V_{OUT} = 0.795 \times (1 + \frac{R_{FBT}}{R_{FBB}}) \]  

(4)

Rearranging terms; the ratio of the feedback resistors for a desired output voltage is:

\[ \frac{R_{FBT}}{R_{FBB}} = \frac{V_{OUT}}{0.795} - 1 \]  

(5)

These resistors must generally be chosen from values in the range of 1.0 kΩ to 10.0 kΩ.

For \( V_{OUT} = 0.8 \) V the FB pin can be connected to the output directly and \( R_{FBB} \) can be set to 8.06 kΩ to provide minimum output load.

Table 1 lists the values for \( R_{FBT} \), and \( R_{FBB} \).

### Table 1. Typical Application Bill of Materials

<table>
<thead>
<tr>
<th>REF DES</th>
<th>DESCRIPTION</th>
<th>CASE SIZE</th>
<th>MANUFACTURER</th>
<th>MANUFACTURER P/N</th>
</tr>
</thead>
<tbody>
<tr>
<td>U1</td>
<td>SIMPLE SWITCHER</td>
<td>PFM-11</td>
<td>Texas Instruments</td>
<td>LMZ23610TZ</td>
</tr>
<tr>
<td>C1,6 (OPT)</td>
<td>0.047 µF, 50 V, X7R</td>
<td>1206</td>
<td>Yageo America</td>
<td>CC1206KR79B0473</td>
</tr>
<tr>
<td>C9,2,3,4</td>
<td>10 µF, 50 V, X7R</td>
<td>1210</td>
<td>Taiyo Yuden</td>
<td>UMK3250J106MM-T</td>
</tr>
<tr>
<td>CIN5 (OPT)</td>
<td>CAP, AL, 150 µF, 50 V</td>
<td>Radial G</td>
<td>Panasonic</td>
<td>EEE-FK1H151P</td>
</tr>
<tr>
<td>C1,5 (OPT)</td>
<td>0.047 µF, 50 V, X7R</td>
<td>1206</td>
<td>Yageo America</td>
<td>CC1206KR79B0473</td>
</tr>
<tr>
<td>C2 (OPT)</td>
<td>47 µF, 10 V, X7R</td>
<td>1210</td>
<td>Murata</td>
<td>GRM32ER61A476KE20L</td>
</tr>
<tr>
<td>C3,4</td>
<td>330 µF, 6.3 V, 0.015 Ω</td>
<td>CAPSMT_6_UE</td>
<td>Kemet</td>
<td>T520D337M006ATE015</td>
</tr>
<tr>
<td>RFBT</td>
<td>3.32 kΩ</td>
<td>0805</td>
<td>Panasonic</td>
<td>ERJ-6ENF3321V</td>
</tr>
<tr>
<td>RFBF</td>
<td>1.07 kΩ</td>
<td>0805</td>
<td>Panasonic</td>
<td>ERJ-6ENF1071V</td>
</tr>
<tr>
<td>RSYNC</td>
<td>1.50 kΩ</td>
<td>0805</td>
<td>Vishay Dale</td>
<td>CRCW0805K50FKEA</td>
</tr>
<tr>
<td>RENT</td>
<td>42.2 kΩ</td>
<td>0805</td>
<td>Panasonic</td>
<td>ERJ-6ENF4222V</td>
</tr>
<tr>
<td>RENB</td>
<td>12.7 kΩ</td>
<td>0805</td>
<td>Panasonic</td>
<td>ERJ-6ENF1272V</td>
</tr>
<tr>
<td>CSS</td>
<td>0.47 µF, ±10%, X7R, 16 V</td>
<td>0805</td>
<td>AVX</td>
<td>0805YC474KAT2A</td>
</tr>
<tr>
<td>D1 (OPT)</td>
<td>5.1 V, 0.5 W</td>
<td>SOD-123</td>
<td>Diodes Inc.</td>
<td>MMSZ5231BS-7-F</td>
</tr>
</tbody>
</table>

#### 8.2.2.4 Soft-Start Capacitor Selection

Programmable soft-start permits the regulator to slowly ramp to its steady-state operating point after being enabled, thereby reducing current inrush from the input supply and slowing the output voltage rise-time.

Upon turnon, after all UVLO conditions have been passed, an internal 1.6-ms circuit slowly ramps the SS input to implement internal soft-start. If 1.6 ms is an adequate turnon time then the \( C_{SS} \) capacitor can be left unpopulated. Longer soft-start periods are achieved by adding an external capacitor to this input.

Soft-start duration is given by the formula:

\[ t_{SS} = V_{REF} \times C_{SS} / I_{SS} = 0.795 V \times C_{SS} / 50 \mu A \]  

(6)

This equation can be rearranged as follows:

\[ C_{SS} = t_{SS} \times 50 \mu A / 0.795 V \]  

(7)

Using a 0.22-µF capacitor results in 3.5-ms typical soft-start duration; and 0.47 µF results in 7.5 ms typical. 0.47 µF is a recommended initial value.

As the soft-start input exceeds 0.795 V the output of the power stage will be in regulation and the 50-µA current is deactivated. The following conditions will reset the soft-start capacitor by discharging the SS input to ground with an internal current sink.

- The Enable input being pulled low
- A thermal shutdown condition
- \( V_{IN} \) falling below 4.3 V (typical) and triggering the \( V_{CC} \) UVLO

VOUT = 0.795 V × (1 + RFBT / RBB)
8.2.2.5 \( C_{\text{OUT}} \) Selection

None of the required \( C_{\text{OUT}} \) output capacitance is contained within the module. A minimum value ranging from 330 \( \mu \)F for 6-V\( V_{\text{OUT}} \) to 660 \( \mu \)F for 1.2-V\( V_{\text{OUT}} \) applications is required based on the values of internal compensation in the error amplifier. These minimum values can be decreased if the effective capacitor ESR is higher than 15 m\( \Omega \).

A Low ESR (15 m\( \Omega \)) tantalum, organic semiconductor or specialty polymer capacitor types in parallel with a 47-nF X7R ceramic capacitor for high frequency noise reduction is recommended for obtaining lowest ripple. The output capacitor \( C_{\text{OUT}} \) may consist of several capacitors in parallel placed in close proximity to the module. The output voltage ripple of the module depends on the equivalent series resistance (ESR) of the capacitor bank, and can be calculated by multiplying the ripple current of the module by the effective impedance of your chosen output capacitors (for ripple current calculation, see Equation 14). Electrolytic capacitors will have large ESR and lead to larger output ripple than ceramic or polymer types. For this reason a combination of ceramic and polymer capacitors is recommended for low output ripple performance.

The output capacitor assembly must also meet the worst case ripple current rating of \( \Delta i_L \), as calculated in Equation 14 below. Loop response verification is also valuable to confirm closed loop behavior.

For applications with dynamic load steps; the following equation provides a good first pass approximation of \( C_{\text{OUT}} \) for load transient requirements.

\[
C_{\text{OUT}} \geq \frac{I_{\text{step}}}{(\Delta V_{\text{OUT}} - I_{\text{STEP}} \times \text{ESR}) \times \left( \frac{f_{\text{SW}}}{V_{\text{OUT}}} \right)}
\]

For 12 \( V_{\text{IN}} \), 3.3 \( V_{\text{OUT}} \), a transient voltage of 5% of \( V_{\text{OUT}} = 0.165 \) V (\( \Delta V_{\text{OUT}} \)), a 9-A load step (\( I_{\text{STEP}} \)), an output capacitor effective ESR of 3 m\( \Omega \), and a switching frequency of 350 kHz (\( f_{\text{SW}} \)):

\[
C_{\text{OUT}} \geq \frac{9A}{(0.165V - 9A \times 0.003) \times \left( \frac{350e3}{3.3V} \right)}
\]

\[
\geq 615 \mu \text{F}
\]

**NOTE**

The stability requirement for minimum output capacitance must always be met.

One recommended output capacitor combination is two 330-\( \mu \)F, 15-m\( \Omega \) ESR tantalum polymer capacitors connected in parallel with a 47-\( \mu \)F 6.3-V X5R ceramic. This combination provides excellent performance that may exceed the requirements of certain applications. Additionally some small 47-nF ceramic capacitors can be used for high-frequency EMI suppression.

8.2.2.6 \( C_{\text{IN}} \) Selection

The LMZ23610 module contains two internal ceramic input capacitors. Additional input capacitance is required external to the module to handle the input ripple current of the application. The input capacitor can be several capacitors in parallel. This input capacitance must be located in very close proximity to the module. Input capacitor selection is generally directed to satisfy the input ripple current requirements rather than by capacitance value. Input ripple current rating is dictated by the equation:

\[
I_{\text{IN,RMS}} = I_{\text{OUT}} \times \sqrt{D(1-D)}
\]

where

- \( D \equiv V_{\text{OUT}} / V_{\text{IN}} \)

As a point of reference, the worst case ripple current will occur when the module is presented with full load current and when \( V_{\text{IN}} = 2 \times V_{\text{OUT}} \).

Recommended minimum input capacitance is 30-\( \mu \)F X7R (or X5R) ceramic with a voltage rating at least 25% higher than the maximum applied input voltage for the application. TI also recommends to pay attention to the voltage and temperature derating of the capacitor selected.

**NOTE**

Ripple current rating of ceramic capacitors may be missing from the capacitor data sheet and you may have to contact the capacitor manufacturer for this parameter.
If the system design requires a certain minimum value of peak-to-peak input ripple voltage ($\Delta V_{IN}$) to be maintained then the following equation may be used.

$$C_{IN} \geq \frac{I_{OUT} \times D \times (1 - D)}{f_{SW} \times \Delta V_{IN}}$$  \hspace{1cm} (11)

If $\Delta V_{IN}$ is 200 mV or 1.66% of $V_{IN}$ for a 12-V input to 3.3-V output application and $f_{SW} = 350$ kHz then:

$$C_{IN} \geq \frac{10A \times \left(\frac{3.3V}{12V}\right) \times \left(1 - \frac{3.3V}{12V}\right)}{350 \text{ kHz} \times 200 \text{ mV}} \geq 28 \mu F$$  \hspace{1cm} (12)

Additional bulk capacitance with higher ESR may be required to damp any resonant effects of the input capacitance and parasitic inductance of the incoming supply lines. The LMZ23610 typical applications schematic and evaluation board include a 150-$\mu$F 50-V aluminum capacitor for this function. There are many situations where this capacitor is not necessary.

### 8.2.2.7 Discontinuous Conduction and Continuous Conduction Mode Selection

The approximate formula for determining the DCM/CCM boundary is as follows:

$$I_{DCB} = \frac{(V_{IN} - V_{OUT}) \times D}{2 \times L \times f_{SW}}$$  \hspace{1cm} (13)

The inductor internal to the module is 2.2 $\mu$H. This value was chosen as a good balance between low and high input voltage applications. The main parameter affected by the inductor is the amplitude of the inductor ripple current ($\Delta i_L$). $\Delta i_L$ can be calculated with:

$$\Delta i_L = \frac{(V_{IN} - V_{OUT}) \times D}{L \times f_{SW}}$$

where

- $V_{IN}$ is the maximum input voltage
- $f_{SW}$ is typically 359 kHz

If the output current $I_{OUT}$ is determined by assuming that $I_{OUT} = i_L$, the higher and lower peak of $\Delta i_L$ can be determined.
8.2.3 Application Curves

**Figure 53. Efficiency**

- $V_{IN} = 24$ V, $V_{OUT} = 3.3$ V

**Figure 54. Thermal Derating Curve**

- $V_{IN} = 24$ V, $V_{OUT} = 3.3$ V

**Figure 55. Radiated EMI (EN 55022)**

- $V_{IN} = 24$ V, $V_{OUT} = 5$ V,
- $I_{OUT} = 10$ A
9 Power Supply Recommendations

The LMZ23610 device is designed to operate from an input voltage supply range between 6 V and 36 V. This input supply must be well regulated and able to withstand maximum input current and maintain a stable voltage. The resistance of the input supply rail must be low enough that an input current transient does not cause a high enough drop at the LMZ23610 supply voltage that can cause a false UVLO fault triggering and system reset. If the input supply is more than a few inches from the LMZ23610, additional bulk capacitance may be required in addition to the ceramic bypass capacitors. The amount of bulk capacitance is not critical, but a 47-μF or 100-μF electrolytic capacitor is a typical choice.

10 Layout

10.1 Layout Guidelines

PC board layout is an important part of DC-DC converter design. Poor board layout can disrupt the performance of a DC-DC converter and surrounding circuitry by contributing to EMI, ground bounce and resistive voltage drop in the traces. These can send erroneous signals to the DC-DC converter resulting in poor regulation or instability. Good layout can be implemented by following a few simple design rules. A good layout example is shown in Figure 59.

1. Minimize area of switched current loops.

   From an EMI reduction standpoint, it is imperative to minimize the high di/dt paths during PCB layout as shown in Figure 56 above. The high current loops that do not overlap have high di/dt content that will cause observable high frequency noise on the output pin if the input capacitor (C_{IN}) is placed at a distance away from the LMZ23610. Therefore place C_{IN} as close as possible to the LMZ23610 VIN and PGND exposed pad. This will minimize the high di/dt area and reduce radiated EMI. Additionally, grounding for both the input and output capacitor must consist of a localized top side plane that connects to the PGND exposed pad (EP).

2. Have a single point ground.

   The ground connections for the feedback, soft-start, and enable components must be routed to the AGND pin of the device. This prevents any switched or load currents from flowing in the analog ground traces. If not properly handled, poor grounding can result in degraded load regulation or erratic output voltage ripple behavior. Additionally provide a single point ground connection from pin 4 (AGND) to EP/PGND.

3. Minimize trace length to the FB pin.

   Both feedback resistors, R_{FBT} and R_{FBB} must be located close to the FB pin. Because the FB node is high impedance, maintain the copper area as small as possible. The traces from R_{FBT}, R_{FBB} must be routed away from the body of the LMZ23610 to minimize possible noise pickup.

4. Make input and output bus connections as wide as possible.

   This reduces any voltage drops on the input or output of the converter and maximizes efficiency. To optimize voltage accuracy at the load, ensure that a separate feedback voltage sense trace is made to the load. Doing so will correct for voltage drops and provide optimum output accuracy.

5. Provide adequate device heat-sinking.

   Use an array of heat-sinking vias to connect the exposed pad to the ground plane on the bottom PCB layer. If the PCB has multiple copper layers, these thermal vias can also be connected to inner layer heat-spreading ground planes. For best results use a 10 x 10 via array or larger with a minimum via diameter of 8 mil thermal vias spaced 46.8 mil (1.5 mm). Ensure enough copper area is used for heat-sinking to keep the junction temperature below 125°C.
10.2 Layout Examples

Figure 56. Critical Current Loops to Minimize

Figure 57. PCB Layout Guide
Layout Examples (continued)

Figure 58. Top View of Evaluation PCB

Figure 59. Bottom View of Evaluation PCB
10.3 Power Dissipation and Thermal Considerations

When calculating module dissipation use the maximum input voltage and the average output current for the application. Many common operating conditions are provided in the characteristic curves such that less common applications can be derived through interpolation. In all designs, the junction temperature must be kept below the rated maximum of 125°C.

For the design case of $V_{IN} = 12\, \text{V}$, $V_{OUT} = 3.3\, \text{V}$, $I_{OUT} = 10\, \text{A}$, and $T_{A-MAX} = 50\, ^\circ\text{C}$, the module must see a thermal resistance from case to ambient ($\theta_{CA}$) of less than:

$$\theta_{CA} < \frac{T_{J-MAX} - T_{A-MAX}}{P_{IC-LOSS}} - \theta_{JC}$$  \hspace{1cm} (15)

Given the typical thermal resistance from junction to case ($\theta_{JC}$) to be 1.0°C/W. Use the 85°C power dissipation curves in the Typical Characteristics section to estimate the $P_{IC-LOSS}$ for the application being designed. In this application it is 5.3 W.

$$\theta_{CA} < \frac{125^\circ\text{C} - 50^\circ\text{C}}{3.9\, \text{W}} - 1.0\, \frac{^\circ\text{C}}{\text{W}} < 18.23\, \frac{^\circ\text{C}}{\text{W}}$$  \hspace{1cm} (16)

To reach $\theta_{CA} = 13.15$, the PCB is required to dissipate heat effectively. With no airflow and no external heat-sink, a good estimate of the required board area covered by 2-oz. copper on both the top and bottom metal layers is:

$$\text{Board Area}_{cm^2} \geq \frac{500\, ^\circ\text{C} \times cm^2}{\theta_{CA}\, \text{W}}$$  \hspace{1cm} (17)

As a result, approximately 38.02 square cm of 2-oz. copper on top and bottom layers is the minimum required area for the example PCB design. This is 6.16 × 6.16 cm (2.42 × 2.42 in) square. The PCB copper heat sink must be connected to the exposed pad. For best performance, use approximately 100, 8 mil thermal vias spaced 59 mil (1.5 mm) apart connect the top copper to the bottom copper.

Another way to estimate the temperature rise of a design is using $\theta_{JA}$. An estimate of $\theta_{JA}$ for varying heat sinking copper areas and airflows can be found in the typical applications curves. If our design required the same operating conditions as before but had 225 LFPM of airflow. We locate the required $\theta_{JA}$ of

$$\theta_{JA} < \frac{T_{J-MAX} - T_{A-MAX}}{P_{IC-LOSS}}$$

$$\theta_{JA} < \frac{(125 - 50)\, ^\circ\text{C}}{3.9\, \text{W}} < 19.23\, \frac{^\circ\text{C}}{\text{W}}$$  \hspace{1cm} (18)

On the $\theta_{JA}$ vs copper heatsinking curve, the copper area required for this application is now only 2 square inches. The airflow reduced the required heat sinking area by a factor of three.

To reduce the heat sinking copper area further, this package is compatible with D3-PAK surface mount heat sinks.

For an example of a high thermal performance PCB layout for SIMPLE SWITCHER power modules, refer to AN-2093 (SNVA460), AN-2084 (SNVA456), AN-2125 (SNVA473), AN-2020 (SNVA419) and AN-2026 (SNVA424).

10.4 Power Module SMT Guidelines

The recommendations below are for a standard module surface mount assembly

- Land Pattern — Follow the PCB land pattern with either soldermask defined or non-soldermask defined pads
- Stencil Aperture
  - For the exposed die attach pad (DAP), adjust the stencil for approximately 80% coverage of the PCB land pattern
  - For all other I/O pads use a 1:1 ratio between the aperture and the land pattern recommendation
- Solder Paste — Use a standard SAC Alloy such as SAC 305, type 3 or higher
- Stencil Thickness — 0.125 to 0.15mm
- Reflow — Refer to solder paste supplier recommendation and optimized per board size and density
- Refer to Design Summary LMZ1xxx and LMZ2xxx Power Modules Family (SNAA214) for reflow information
Power Module SMT Guidelines (continued)

- Maximum number of reflows allowed is one

![Sample Reflow Profile](image)

**Figure 60. Sample Reflow Profile**

**Table 2. Sample Reflow Profile Table**

<table>
<thead>
<tr>
<th>PROBE</th>
<th>MAX TEMP (°C)</th>
<th>REACHED MAX TEMP</th>
<th>TIME ABOVE 235°C</th>
<th>REACHED 235°C</th>
<th>TIME ABOVE 245°C</th>
<th>REACHED 245°C</th>
<th>TIME ABOVE 260°C</th>
<th>REACHED 260°C</th>
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<tr>
<td>1</td>
<td>242.5</td>
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<td>0.49</td>
<td>6.39</td>
<td>0.00</td>
<td>–</td>
<td>0.00</td>
<td>–</td>
</tr>
<tr>
<td>2</td>
<td>242.5</td>
<td>7.10</td>
<td>0.55</td>
<td>6.31</td>
<td>0.00</td>
<td>7.10</td>
<td>0.00</td>
<td>–</td>
</tr>
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<td>3</td>
<td>241.0</td>
<td>7.09</td>
<td>0.42</td>
<td>6.44</td>
<td>0.00</td>
<td>–</td>
<td>0.00</td>
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</tr>
</tbody>
</table>
11 Device and Documentation Support

11.1 Device Support

11.1.1 Third-Party Products Disclaimer
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11.1.2 Development Support
For developmental support, see the following:

11.2 Documentation Support

11.2.1 Related Documentation
For related documentation, see the following:
• AN-2027 Inverting Application for the LMZ14203 SIMPLE SWITCHER Power Module, (SNVA425)
• Absolute Maximum Ratings for Soldering, (SNOA549)
• AN-2024 LMZ1420x / LMZ1200x Evaluation Board (SNVA422)
• AN-2085 LMZ23605/03, LMZ22005/03 Evaluation Board (SNVA457)
• AN-2054 Evaluation Board for LM10000 - PowerWise AVS System Controller (SNVA437)
• AN-2020 Thermal Design By Insight, Not Hindsight (SNVA419)
• AN-2093 LMZ23610/8/6 and LMZ22010/8/6 Current Sharing Evaluation Board (SNVA460)
• AN-2026 Effect of PCB Design on Thermal Performance of SIMPLE SWITCHER Power Modules (SNVA424)
• Design Summary LMZ1xxx and LMZ2xxx Power Modules Family (SNAA214)

11.3 Receiving Notification of Documentation Updates
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Design Support TI's Design Support Quickly find helpful E2E forums along with design support tools and contact information for technical support.

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11.6 Electrostatic Discharge Caution
These devices have limited built-in ESD protection. The leads should be shorted together or the device placed in conductive foam during storage or handling to prevent electrostatic damage to the MOS gates.
11.7 Glossary

SLYZ022 — Ti Glossary.

This glossary lists and explains terms, acronyms, and definitions.

12 Mechanical, Packaging, and Orderable Information

The following pages include mechanical, packaging, and orderable information. This information is the most current data available for the designated devices. This data is subject to change without notice and revision of this document. For browser-based versions of this data sheet, refer to the left-hand navigation.
## PACKAGING INFORMATION

<table>
<thead>
<tr>
<th>Orderable Device</th>
<th>Status (1)</th>
<th>Package Type</th>
<th>Package Drawing</th>
<th>Pins</th>
<th>Eco Plan (2)</th>
<th>Lead/Ball Finish</th>
<th>MSL Peak Temp (3)</th>
<th>Op Temp (°C)</th>
<th>Device Marking (4/5)</th>
<th>Samples</th>
</tr>
</thead>
<tbody>
<tr>
<td>LMZ23610TZ/NOPB</td>
<td>ACTIVE</td>
<td>PFM</td>
<td>NDY</td>
<td>11</td>
<td>Green (RoHS &amp; no Sb/Br)</td>
<td>CU SN</td>
<td>Level-3-245C-168 HR</td>
<td>-40 to 85</td>
<td>LMZ23610</td>
<td>Samples</td>
</tr>
<tr>
<td>LMZ23610TZE/NOPB</td>
<td>ACTIVE</td>
<td>PFM</td>
<td>NDY</td>
<td>250</td>
<td>Green (RoHS &amp; no Sb/Br)</td>
<td>CU SN</td>
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<td>-40 to 85</td>
<td>LMZ23610</td>
<td>Samples</td>
</tr>
</tbody>
</table>

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- **LIFEBUY:** TI has announced that the device will be discontinued, and a lifetime-buy period is in effect.
- **NRND:** Not recommended for new designs. Device is in production to support existing customers, but TI does not recommend using this part in a new design.
- **PREVIEW:** Device has been announced but is not in production. Samples may or may not be available.
- **OBsolete:** TI has discontinued the production of the device.

(2) Eco Plan - The planned eco-friendly classification: Pb-Free (RoHS), Pb-Free (RoHS Exempt), or Green (RoHS & no Sb/Br) - please check [http://www.ti.com/productcontent](http://www.ti.com/productcontent) for the latest availability information and additional product content details.
- **Pb-Free (RoHS):** TI’s terms “Lead-Free” or “Pb-Free” mean semiconductor products that are compatible with the current RoHS requirements for all 6 substances, including the requirement that lead not exceed 0.1% by weight in homogeneous materials. Where designed to be soldered at high temperatures, TI Pb-Free products are suitable for use in specified lead-free processes.
- **Pb-Free (RoHS Exempt):** This component has a RoHS exemption for either 1) lead-based flip-chip solder bumps used between the die and package, or 2) lead-based die adhesive used between the die and leadframe. The component is otherwise considered Pb-Free (RoHS compatible) as defined above.
- **Green (RoHS & no Sb/Br):** TI defines "Green" to mean Pb-Free (RoHS compatible), and free of Bromine (Br) and Antimony (Sb) based flame retardants (Br or Sb do not exceed 0.1% by weight in homogeneous material)

(3) **MSL, Peak Temp.** - The Moisture Sensitivity Level rating according to the JEDEC industry standard classifications, and peak solder temperature.

(4) There may be additional marking, which relates to the logo, the lot trace code information, or the environmental category on the device.

(5) Multiple Device Markings will be inside parentheses. Only one Device Marking contained in parentheses and separated by a "~" will appear on a device. If a line is indented then it is a continuation of the previous line and the two combined represent the entire Device Marking for that device.

(6) **Lead/Ball Finish** - Orderable Devices may have multiple material finish options. Finish options are separated by a vertical ruled line. Lead/Ball Finish values may wrap to two lines if the finish value exceeds the maximum column width.

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TAPE AND REEL INFORMATION

*All dimensions are nominal

<table>
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<th>Device</th>
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<th>B0 (mm)</th>
<th>K0 (mm)</th>
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<th>W (mm)</th>
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A0 Dimension designed to accommodate the component width
B0 Dimension designed to accommodate the component length
K0 Dimension designed to accommodate the component thickness
W Overall width of the carrier tape
P1 Pitch between successive cavity centers
**TAPE AND REEL BOX DIMENSIONS**

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- **RoHS Exempt**: TI defines "RoHS Exempt" to mean products that contain lead but are compliant with EU RoHS pursuant to a specific EU RoHS exemption.

- **Green**: TI defines "Green" to mean the content of Chlorine (Cl) and Bromine (Br) based flame retardants meet JS709B low halogen requirements of <=1000ppm threshold. Antimony trioxide based flame retardants must also meet the <=1000ppm threshold requirement.

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<th>B0 (mm)</th>
<th>K0 (mm)</th>
<th>P1 (mm)</th>
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- **K0**: Dimension designed to accommodate the component thickness
- **W**: Overall width of the carrier tape
- **P1**: Pitch between successive cavity centers

---

**TAPE DIMENSIONS**

- **K0**: Cavity width
- **P1**: Reel diameter

**QUADRANT ASSIGNMENTS FOR PIN 1 ORIENTATION IN TAPE**

- **Q1**
- **Q2**
- **Q3**
- **Q4**

*www.ti.com 27-May-2018*
# TAPE AND REEL BOX DIMENSIONS

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<table>
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<tr>
<th>Device</th>
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