LMH6504 Wideband, Low Power, Variable Gain Amplifier

Check for Samples: LMH6504

FEATURES

- **V_S = ±5V, T_A = 25°C, R_F = 1 KΩ, R_G = 100Ω, R_L = 100Ω, A_V = A_{VMAX} = 9.7V/V, Typical values unless specified.**
- **−3 dB BW 150 MHz**
- **Gain control BW 150 MHz**
- **Adjustment range (<10 MHz) 80 dB**
- **Output offset voltage ±55 mV**
- **Gain matching (limit) ±0.42 dB**
- **Supply voltage range 7V to 12V**
- **Slew rate (inverting) 1500 V/µs**
- **Supply Current (no load) 11 mA**
- **Linear Output Current ±60 mA**
- **Output Voltage Swing ±2.2V**
- **Input Noise Voltage 4.4 nV/$\sqrt{Hz}$**
- **Input Noise Current 2.6 pA/$\sqrt{Hz}$**
- **THD (20 MHz, R_L = 100Ω, V_O = 2 V_{PP}) −45 dBc**
- **Replacement for CLC5523**

APPLICATIONS

- **Variable attenuator**
- **AGC**
- **Voltage controlled filter**
- **Video imaging processing**

DESCRIPTION

The LMH™6504 is a wideband DC coupled voltage controlled gain stage followed by a high-speed current feedback Op Amp which can directly drive a low impedance load. Gain adjustment range is 80 dB for up to 10 MHz by varying the gain control input voltage, V_G.

Maximum gain is set by external components, and the gain can be reduced all the way to cut-off. Power consumption is 110 mW with a speed of 150 MHz and a gain control bandwidth (BW) of 150 MHz. Output referred DC offset voltage is less than 55 mV over the entire gain control voltage range. Device-to-device gain matching is within ±0.42 dB at maximum gain. Furthermore, gain is tested over a wide range. The output current feedback Op Amp allows high frequency large signals (Slew Rate > 1500 V/µs) and can also drive a heavy load current (60 mA). Near ideal input characteristics (i.e. low input bias current, low offset, low pin 3 resistance) enable the device to be easily configured as an inverting amplifier as well (see Application Information section for details).

To provide ease of use when working with a single supply, V_G range is set to be from 0V to +2V relative to the ground pin potential (pin 4). V_G input impedance is high in order to ease drive requirement. In single supply operation, the ground pin is tied to a "virtual" half supply.

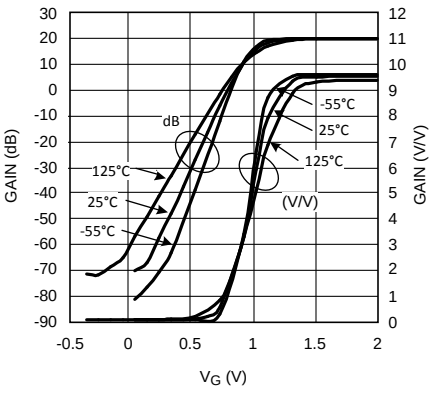


Figure 1. Gain vs. V_G

Typical Application

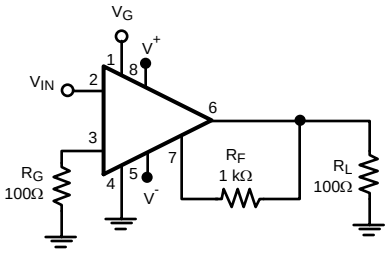


Figure 2. A_{VMAX} = 9.7 V/V

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PRODUCTION DATA information is current as of publication date. Products conform to specifications per the terms of the Texas Instruments standard warranty. Production processing does not necessarily include testing of all parameters.

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DESCRIPTION CONTINUED

LMH6504 gain control is linear in dB for a large portion of the total gain control range. This makes the device suitable for AGC applications. For linear gain control applications, see the LMH6503 data sheet.

The combination of minimal external components and small outline packages (SOIC and VSSOP) allows the LMH6504 to be used in space-constrained applications.

These devices have limited built-in ESD protection. The leads should be shorted together or the device placed in conductive foam during storage or handling to prevent electrostatic damage to the MOS gates.

Absolute Maximum Ratings (1)

ESD Tolerance (2):	
Human Body Model	1000V
Machine Model	100V
Input Current	±10 mA
Output Current	120 mA (3)
Supply Voltages (V^+ - V^-)	12.6V
Voltage at Input/ Output pins	V^+ +0.8V, V^- −0.8V
Storage Temperature Range	−65°C to 150°C
Junction Temperature	150°C
Soldering Information:	
Infrared or Convection (20 sec)	235°C
Wave Soldering (10 sec)	260°C

(1) Absolute Maximum Ratings indicate limits beyond which damage to the device may occur. Operating Ratings indicate conditions for which the device is intended to be functional, but specific performance is not ensured. For specifications, see the Electrical Characteristics.
(2) Human Body Model, applicable std. MIL-STD-883, Method 3015.7. Machine Model, applicable std. JESD22-A115-A (ESD MM std. of JEDEC). Field-Induced Charge-Device Model, applicable std. JESD22-C101-C (ESD FICDM std. of JEDEC).
(3) The maximum output current (I_{OUT}) is determined by device power dissipation limitations or value specified, whichever is lower.

Operating Ratings

Supply Voltages (V^+ - V^-)		7V to 12V
Temperature Range (1)		−40°C to +85°C
Thermal Resistance:	(θ_{JC})	(θ_{JA})
8-Pin SOIC	60	165
8-Pin VSSOP	65	235

(1) The maximum power dissipation is a function of $T_{J(MAX)}$, θ_{JA}. The maximum allowable power dissipation at any ambient temperature is $P_D = (T_{J(MAX)} – T_A)/ \theta_{JA}$. All numbers apply for packages soldered directly onto a PC Board.

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Electrical Characteristics (1)

Unless otherwise specified, all limits are specified for T_A = 25°C, V_S = ±5V, A_{VMAX} = 9.7 V/V, R_F = 1 kΩ, R_G = 100Ω, V_{IN} = ±0.1V, R_L = 100Ω, V_G = +2V. **Boldface** limits apply at the temperature extremes.

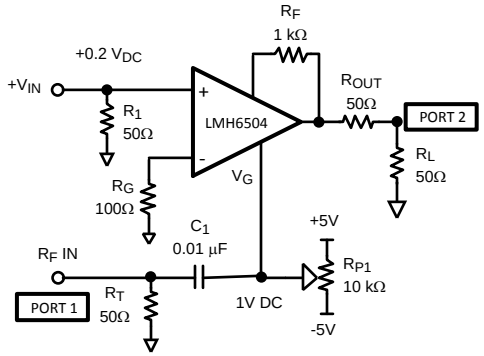
Symbol	Parameter	Conditions	Min (2)	Typ (2)	Max (2)	Units
Frequency Domain Response						
BW	-3dB Bandwidth	V_{OUT} < 1 V_{PP}		150		MHz
		V_{OUT} < 4 V_{PP}, A_{VMAX} = 100		58		
GF	Gain Flatness	V_{OUT} < 1 V_{PP} 0.9V ≤ V_G ≤ 2V, ±0.2 dB		40		MHz
Att Range	Flat Band (Relative to Max Gain) Attenuation Range (3)	±0.2 dB Flatness, f < 30 MHz		26		dB
		±0.1 dB Flatness, f < 30 MHz		9.5		
BW Control	Gain control Bandwidth	V_G = 1V (4)		150		MHz
CT (dB)	Feed-through	V_G = 0V, 30 MHz (Output/Input)		−53		dB
GR	Gain Adjustment Range	f < 10 MHz		80		dB
		f < 30 MHz		73		
Time Domain Response						
t_r, t_f	Rise and Fall Time	0.5V Step		2.1		ns
OS %	Overshoot			20		%
SR	Slew Rate (5)	4V Step, Non Inverting		800		V/µs
		4V Step, Inverting		1500		
Distortion & Noise Performance						
HD2	2nd Harmonic Distortion	$2V_{PP}$, 20 MHz		−47		dBc
HD3	3rd Harmonic Distortion			–55		
THD	Total Harmonic Distortion			−45		
En tot	Total Equivalent Input Noise	f > 1 MHz, R_{SOURCE} = 50Ω		4.4		nV/√Hz
I_N	Input Noise Current	f > 1 MHz		2.6		pA/√Hz
DG	Differential Gain	f = 4.43 MHz, R_L = 100Ω		0.45		%
DP	Differential Phase			0.13		deg

(1) Electrical Table values apply only for factory testing conditions at the temperature indicated. Factory testing conditions result in very limited self-heating of the device such that $T_J = T_A$. No parametric performance is indicated in the electrical tables under conditions of internal self-heating where $T_J > T_A$.

(2) Typical values represent the most likely parametric norm as determined at the time of characterization. Actual typical values may vary over time and will also depend on the application and configuration. The typical values are not tested on shipped production material.

(3) Flat Band Attenuation (Relative To Max Gain) Range Definition: Specified as the attenuation range from maximum which allows gain flatness specified (either ±0.2dB or ±0.1dB), relative to A_{VMAX} gain. For example, for f < 30 MHz, here are the Flat Band Attenuation ranges:±0.2 dB: 19.7 dB down to -6.3 dB = 26 dB range±0.1 dB: 19.7 dB down to 10.2 dB = 9.5 dB range

(4) Gain control frequency response schematic:



(5) Slew rate is the average of the rising and falling slew rates.

Electrical Characteristics[1] (continued)

Unless otherwise specified, all limits are specified for T_A = 25°C, V_S = ±5V, A_{VMAX} = 9.7 V/V, R_F = 1 kΩ, R_G = 100Ω, V_{IN} = ±0.1V, R_L = 100Ω, V_G = +2V. **Boldface** limits apply at the temperature extremes.

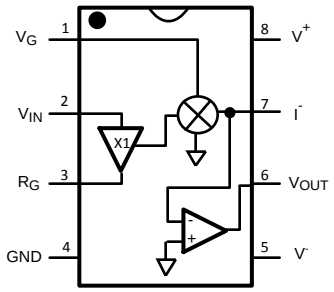
Symbol	Parameter	Conditions	Min [2]	Typ [2]	Max [2]	Units
DC & Miscellaneous Performance						
GACCU	Gain Accuracy (See Application Note)	V_G = 2.0V		0	±0.45	dB
		0.8V < V_G < 2V		±0.33	±3.9	
G Match	Gain Matching (See Application Note	V_G = 2.0V		—	±0.42	dB
		0.8V < V_G < 2V		—	+2.8/−4.2	
K	Gain Multiplier (See Application Notes)		0.920 **0.916**	0.965	1.01 **1.02**	V/V
V_{IN} NL	Input Voltage Range	R_G Open		±3.2		V
V_{IN} L		R_G = 100Ω	±0.48 **±0.40**	±0.68		
I_{RG_MAX}	R_G Current	Pin 3	±4.8 **±4.0**	±6.8		mA
I_{BIAS}	Bias Current	Pin 2 [6]		−1.4	−3.5 **−3.7**	µA
TC I_{BIAS}	Bias Current Drift	Pin 2 [7] [8]		±200		pA/°C
R_{IN}	Input Resistance	Pin 2		7		MΩ
C_{IN}	Input Capacitance	Pin 2		2.8		pF
I_{VG}	V_G Bias Current	Pin 1, V_G = 2V [6]		0.9		µA
TC I_{VG}	V_G Bias Drift	Pin 1 [7]		10		pA/°C
R_{VG}	V_G Input Resistance	Pin 1		25		MΩ
C_{VG}	V_G Input Capacitance	Pin 1		2.8		pF
V_{OUT} L	Output Voltage Range	R_L = 100Ω	±2.0 **±1.7**	±2.2		V
V_{OUT} NL		R_L = Open		±3.1		
R_{OUT}	Output Impedance	DC		0.12		Ω
I_{OUT}	Output Current	V_{OUT} = ±4V from Rails	±60 **±40**	±80		mA
$V_{O\ OFFSET}$	Output Offset Voltage	0V < V_G < 2V		±10	±55 **±70**	mV
+PSRR	+Power Supply Rejection Ratio [9]	Input Referred, 1V change, V_G = 2.2V	–65	–76		dB
−PSRR	−Power Supply Rejection Ratio [9]	Input Referred, 1V change, V_G = 2.2V	–65	–88		dB
I_S	Supply Current	No Load	8.5 **6.5**	11	15 **16**	mA

(6) Positive current corresponds to current flowing into the device.
(7) Drift determined by dividing the change in parameter distribution at temperature extremes by the total temperature change.
(8) Input bias current drift with temperature can be either positive or negative for a given sample.
(9) +PSRR definition: [$|\Delta V_{OUT}/\Delta V^+| / A_V$], −PSRR definition: [$|\Delta V_{OUT}/\Delta V^-| / A_V$] with 0.1V input voltage. ΔV_{OUT} is the change in output voltage with offset shift subtracted out.

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CONNECTION DIAGRAM

8-Pin Package
(Top View)



See Package Number D0008A (SOIC)
and DGK008A (VSSOP)

Typical Performance Characteristics

Unless otherwise specified: V_S = ±5V, T_A = 25°C, V_G = V_{GMAX}, R_F = 1 kΩ, R_G = 100Ω, V_{IN} = 0.1V, input terminated in 50Ω. R_L = 100Ω, Typical values.

Frequency Response Over Temperature

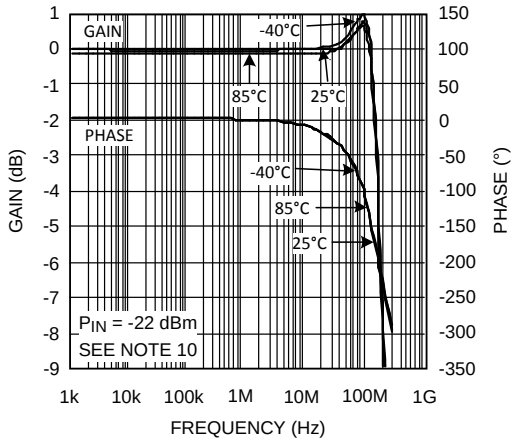


Figure 3.

Frequency Response for Various V_G

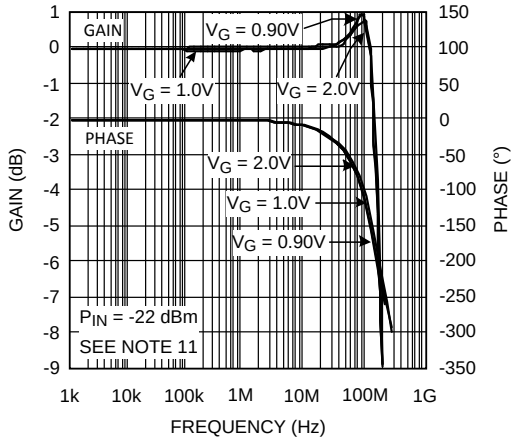


Figure 4.

Frequency Response (A_{VMAX} = 2)

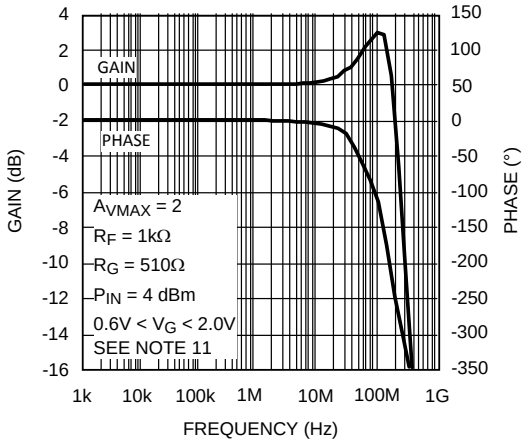


Figure 5.

Inverting Frequency Response

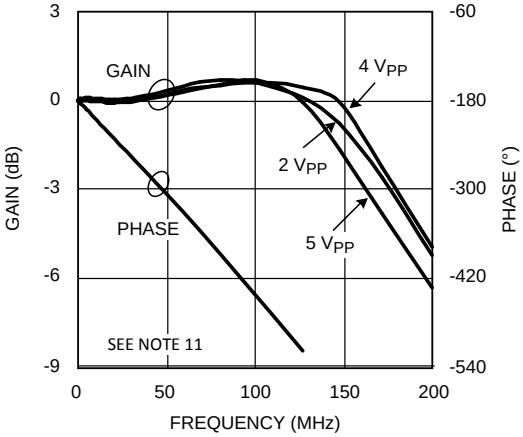


Figure 6.

Frequency Response for Various V_G (A_{VMAX} = 100) (Large Signal)

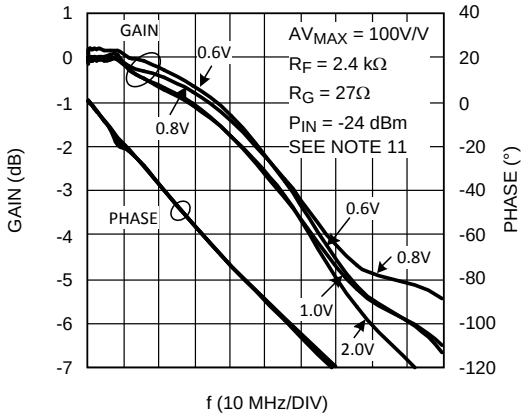


Figure 7.

Frequency Response for Various Amplitudes

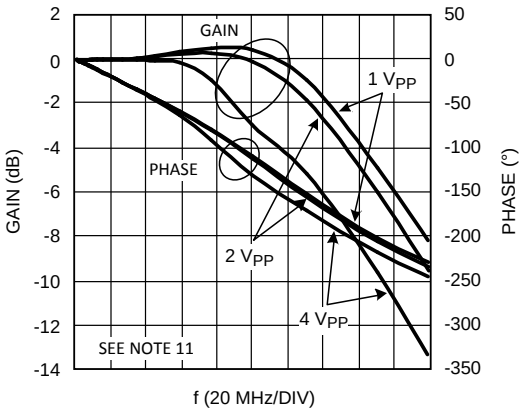


Figure 8.

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Typical Performance Characteristics (continued)

Unless otherwise specified: V_S = ±5V, T_A = 25°C, V_G = V_{GMAX}, R_F = 1 kΩ, R_G = 100Ω, V_{IN} = 0.1V, input terminated in 50Ω. R_L = 100Ω, Typical values.

Gain Control Frequency Response

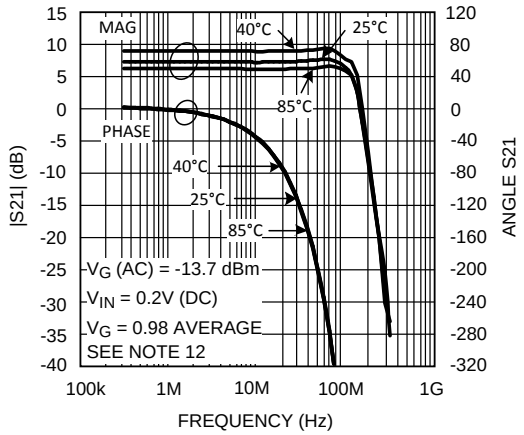


Figure 9.

I_S vs. V_S

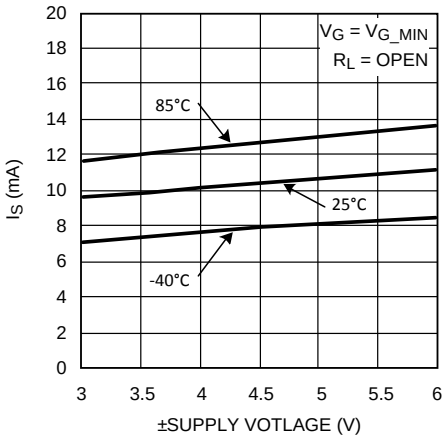


Figure 10.

I_S vs. V_S

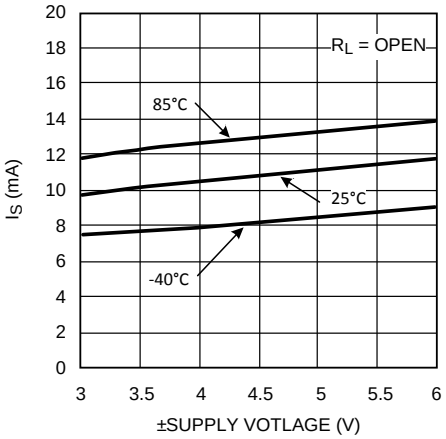


Figure 11.

Input Bias Current vs. V_S

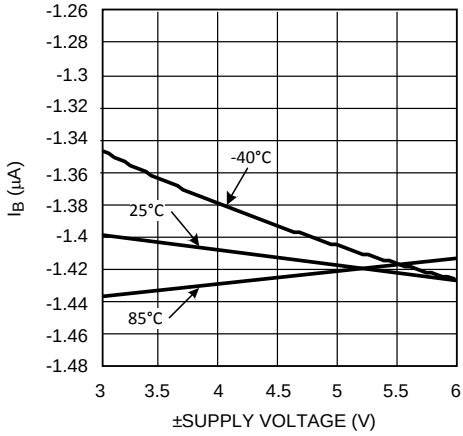


Figure 12.

PSRR

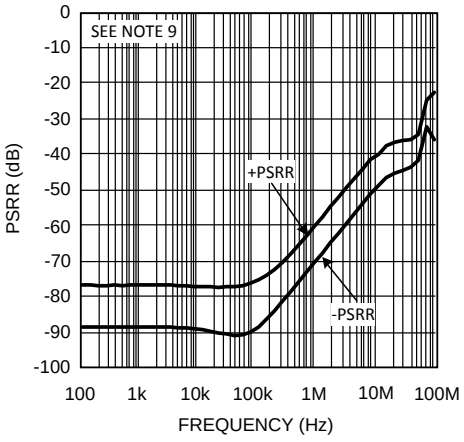


Figure 13.

A_{VMAX} vs. Supply Voltage

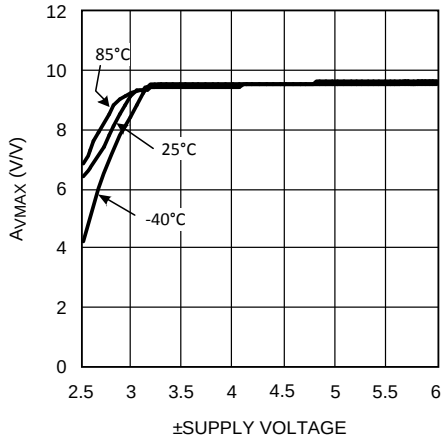


Figure 14.

Typical Performance Characteristics (continued)

Unless otherwise specified: V_S = ±5V, T_A = 25°C, V_G = V_{GMAX}, R_F = 1 kΩ, R_G = 100Ω, V_{IN} = 0.1V, input terminated in 50Ω. R_L = 100Ω, Typical values.

Feed through Isolation for Various A_{VMAX}

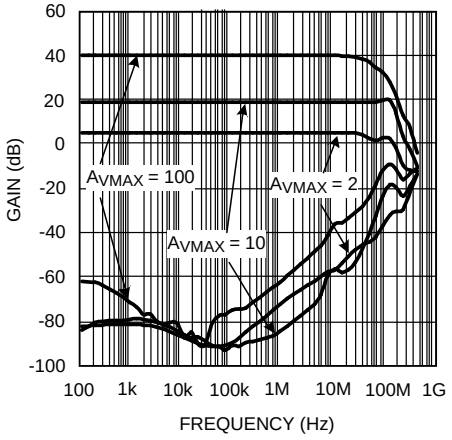


Figure 15.

Gain Variation Over entire Temp Range vs. V_G

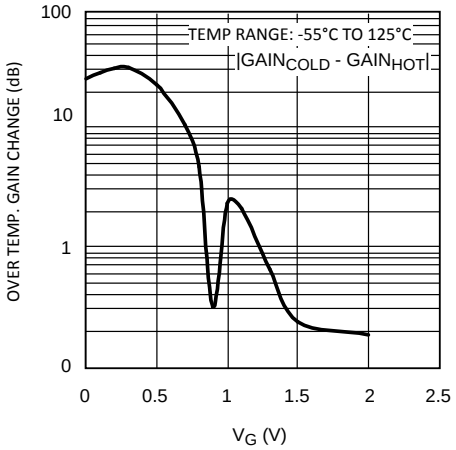


Figure 16.

I_{RG} vs. V_{IN}

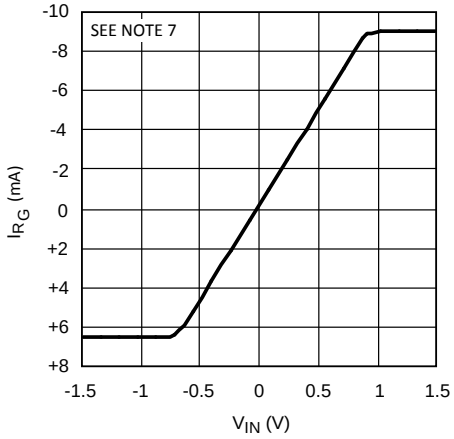


Figure 17.

Gain vs. V_G

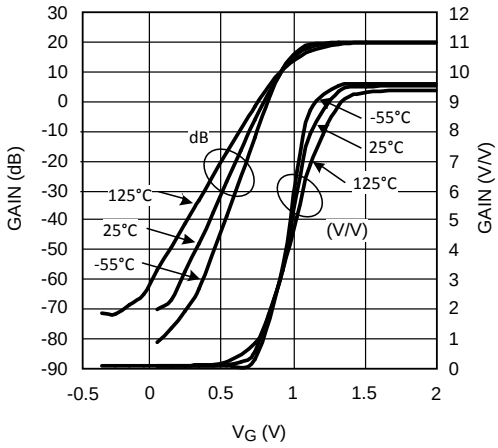


Figure 18.

Gain vs. V_G Including Limits

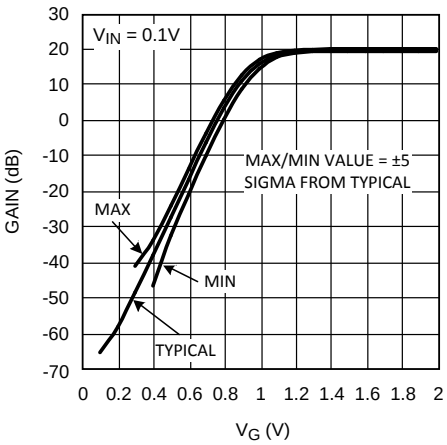


Figure 19.

Output Offset Voltage vs. V_G (Typical Unit #1)

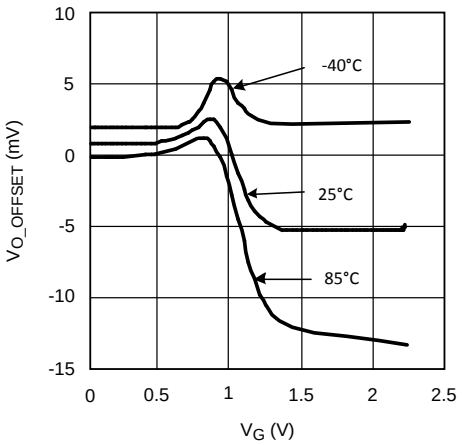


Figure 20.

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Typical Performance Characteristics (continued)

Unless otherwise specified: V_S = ±5V, T_A = 25°C, V_G = V_{GMAX}, R_F = 1 kΩ, R_G = 100Ω, V_{IN} = 0.1V, input terminated in 50Ω. R_L = 100Ω, Typical values.

Output Offset Voltage vs. V_G (Typical Unit #2)

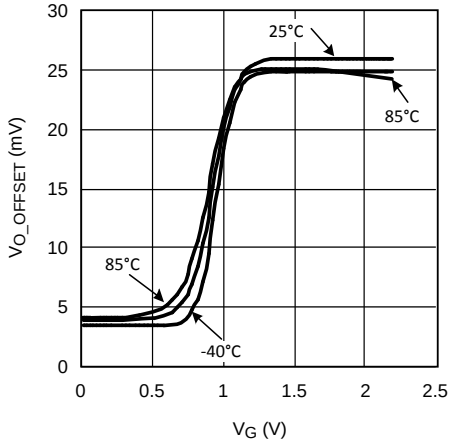


Figure 21.

Output Offset Voltage vs. V_G (Typical Unit #3)

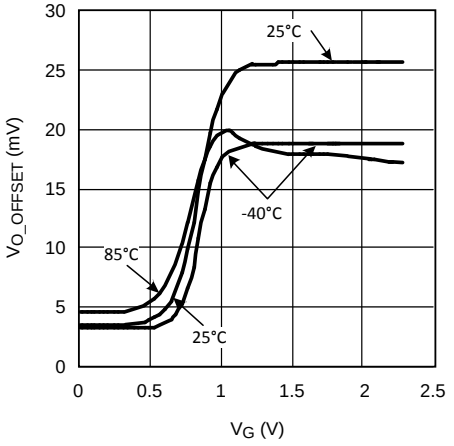


Figure 22.

Distribution of Output Offset Voltage

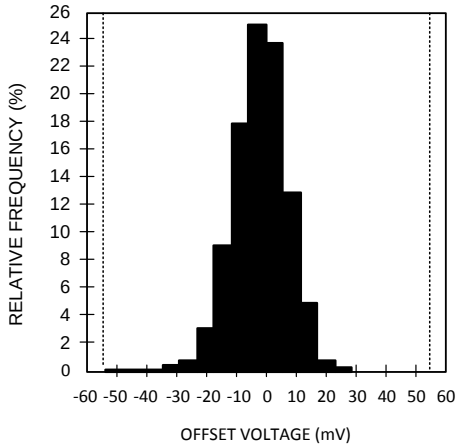


Figure 23.

Output Noise Density vs. Frequency

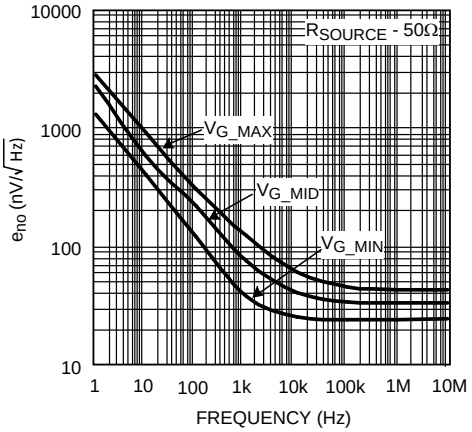


Figure 24.

Output Noise Density vs. Frequency

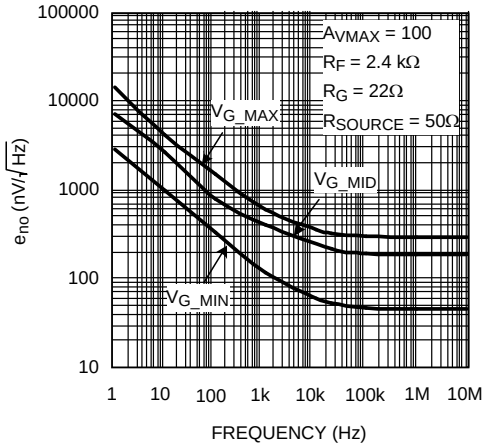


Figure 25.

Output Noise Density vs. Frequency

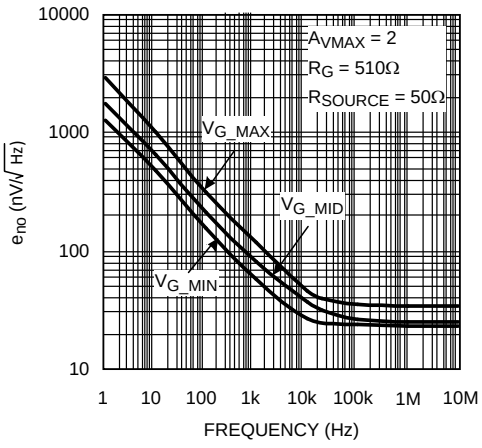


Figure 26.

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Typical Performance Characteristics (continued)

Unless otherwise specified: V_S = ±5V, T_A = 25°C, V_G = V_{GMAX}, R_F = 1 kΩ, R_G = 100Ω, V_{IN} = 0.1V, input terminated in 50Ω. R_L = 100Ω, Typical values.

Input Referred Noise Density vs. Frequency

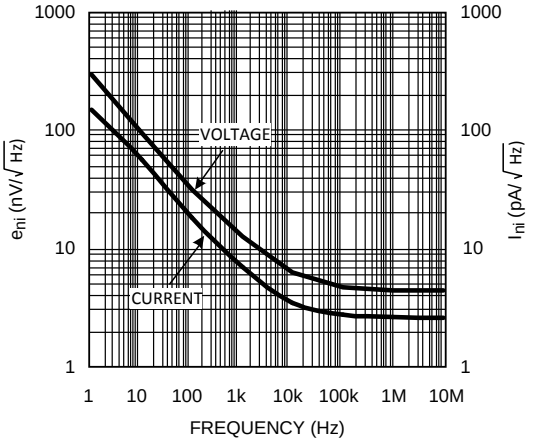


Figure 27.

Output Voltage vs. Output Current (Sinking)

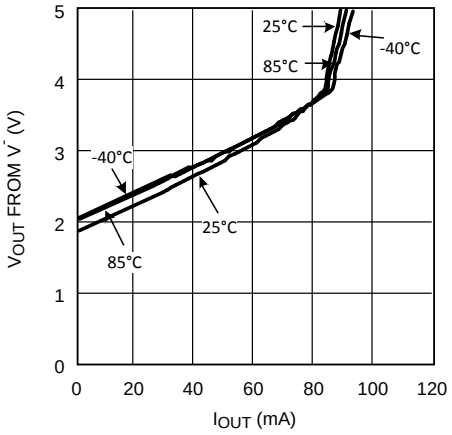


Figure 28.

Output Voltage vs. Output Current (Sourcing)

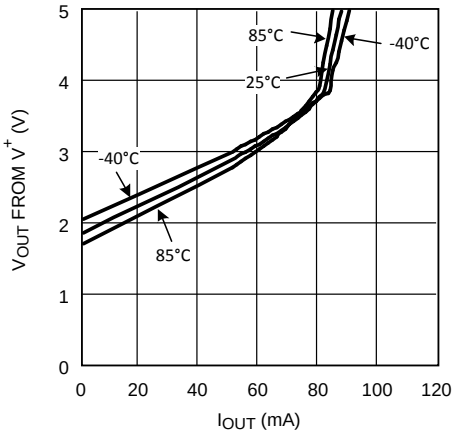


Figure 29.

Distortion vs. Frequency

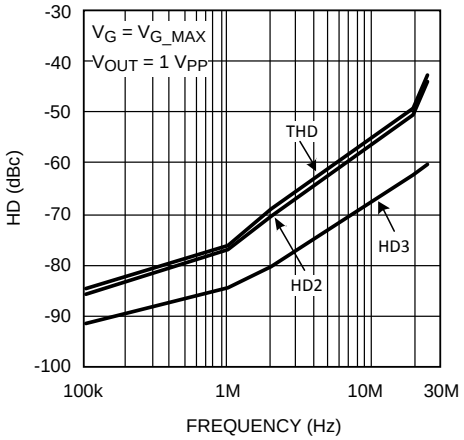


Figure 30.

HD vs. P_{OUT}

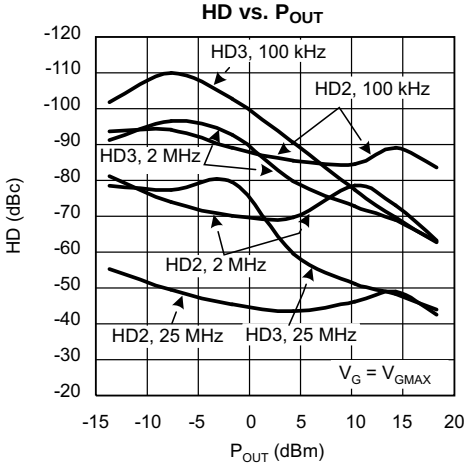


Figure 31.

THD vs. P_{OUT}

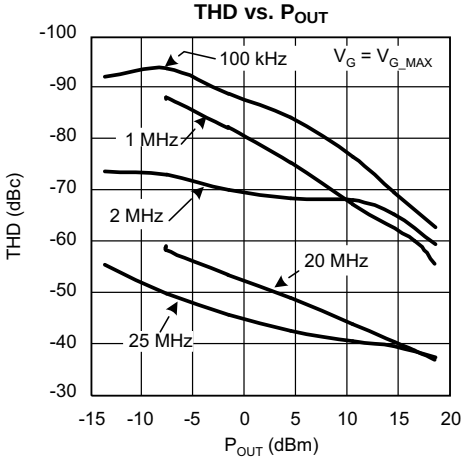


Figure 32.

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Typical Performance Characteristics (continued)

Unless otherwise specified: V_S = ±5V, T_A = 25°C, V_G = V_{GMAX}, R_F = 1 kΩ, R_G = 100Ω, V_{IN} = 0.1V, input terminated in 50Ω. R_L = 100Ω, Typical values.

THD vs. P_{OUT}

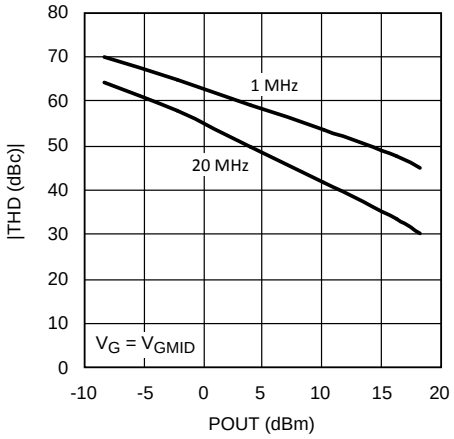


Figure 33.

THD vs. Gain

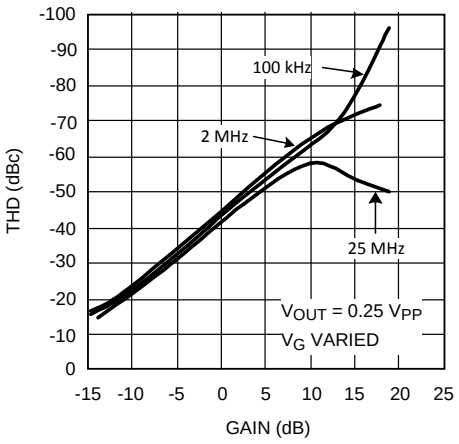


Figure 34.

THD vs. Gain

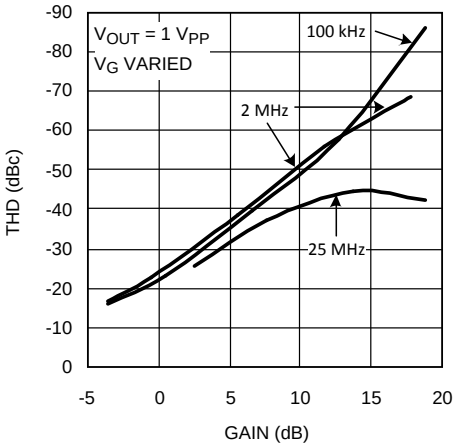


Figure 35.

Differential Gain & Phase

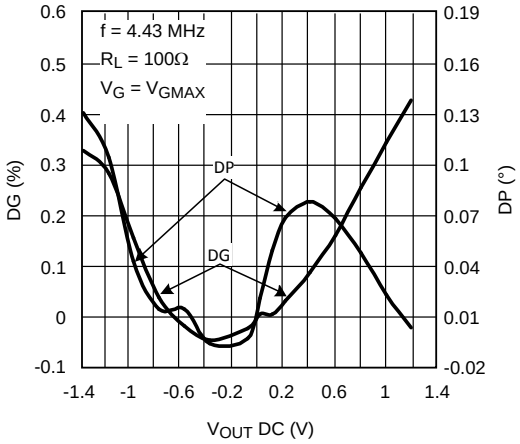


Figure 36.

V_G Bias Current vs. V_G

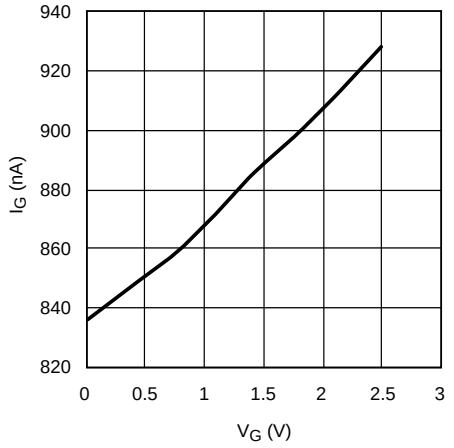


Figure 37.

Output Impedance

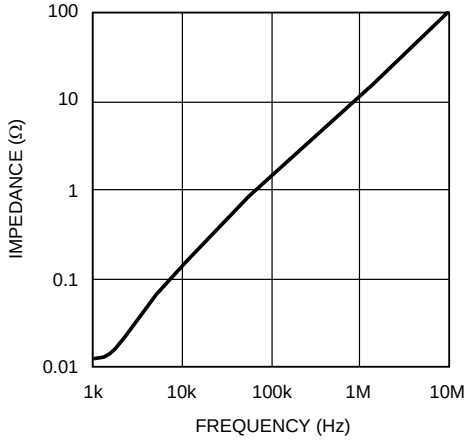


Figure 38.

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Typical Performance Characteristics (continued)

Unless otherwise specified: V_S = ±5V, T_A = 25°C, V_G = V_{GMAX}, R_F = 1 kΩ, R_G = 100Ω, V_{IN} = 0.1V, input terminated in 50Ω. R_L = 100Ω, Typical values.

Step Response Plot

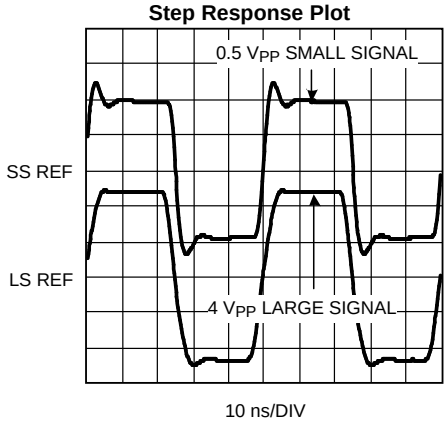


Figure 39.

Step Response Plot

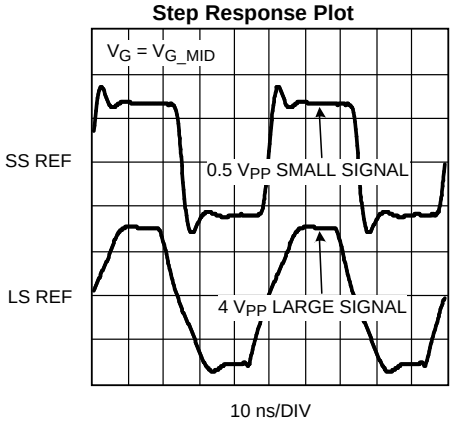


Figure 40.

Gain vs. V_G Step

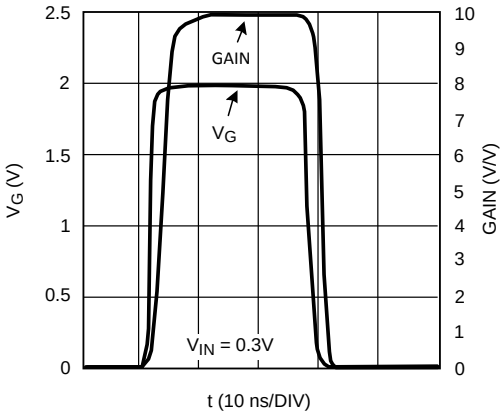


Figure 41.

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APPLICATION INFORMATION

GENERAL DESCRIPTION

The key features of the LMH6504 are:

- Low power
- Broad voltage controlled gain and attenuation range (From A_{VMAX} down to complete cutoff)
- Bandwidth independent, resistor programmable gain range (R_G)
- Broad signal and gain control bandwidths
- Frequency response may be adjusted with R_F
- High impedance signal and gain control inputs

Refer to Figure 42 below. The LMH6504 combines a closed loop input buffer ("X1" Block), a voltage controlled variable gain cell ("MULT" Block) and an output amplifier ("CFA" Block). The input buffer is a transconductance stage whose gain is set by the gain setting resistor, R_G. The output amplifier is a current feedback op amp and is configured as a transimpedance stage whose gain is set by, and is equal to, the feedback resistor, R_F. The maximum gain, A_{VMAX}, of the LMH6504 is defined by the ratio: $K \cdot R_F / R_G$ where "K" is the gain multiplier with a nominal value of 0.965. As the gain control input (V_G) changes over its 0 to 2V range, the gain is adjusted over a range of about 80 dB relative to the maximum set gain.

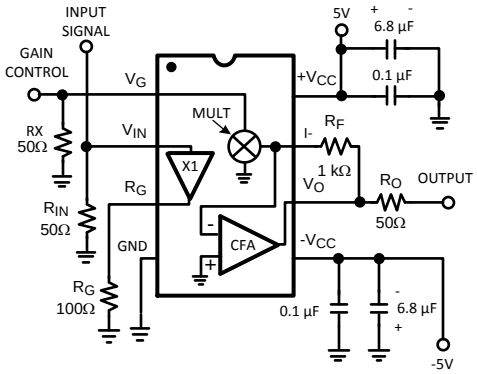


Figure 42. LMH6504 Typical Application and Block Diagram

SETTING THE LMH6504 MAXIMUM GAIN

$$A_{VMAX} = \frac{R_F}{R_G} \cdot K \quad (1)$$

Although the LMH6504 is specified at A_{VMAX} = 9.7V/V, the recommended A_{VMAX} varies between 2 and 100. Higher gains are possible but usually impractical due to output offsets, noise and distortion. When varying A_{VMAX} several tradeoffs are made:

R_G: determines the input voltage range

R_F: determines overall bandwidth

The amount of current which the input buffer can source/sink into R_G is limited and is specified in the I_{RG_MAX} spec. This sets the maximum input voltage:

$$V_{IN}\,(MAX) = I_{R_G\,MAX} \cdot R_G \quad (2)$$

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As the I_{RG_MAX} limit is approached (with increasing input voltage or with lowering of R_G), the device harmonic distortion will increase. Changes in R_F will have a dramatic effect on the small signal bandwidth. The output amplifier of the LMH6504 is a current feedback amplifier (CFA) and its bandwidth is determined by R_F. As with any CFA, doubling the feedback resistor will roughly cut the bandwidth of the device in half. For more about CFA's, see the basic tutorial, OA-20, "Current Feedback Myths Debunked" (SNOA376), or a more rigorous analysis, OA-13, "Current Feedback Amplifier Loop Gain Analysis and Performance Enhancements" (SNOA366).

OTHER CONFIGURATIONS

1) Single Supply Operation

The LMH6504 can be configured for use in a single supply environment. Doing so requires the following:

a. Bias pin 4 and R_G to a "virtual half supply" somewhere close to the middle of V^+ and V^- range. The other end of R_G is tied to pin 3. The "virtual half supply" needs to be capable of sinking and sourcing the expected current flow through R_G.
b. Ensure that V_G can be adjusted from 0V to 2V above the "virtual half supply".
c. Bias the input (pin 2) to make sure that it stays within the range of 1.8V above V^- to 1.8V below V^+ (see "Input voltage Range" specification in the Electrical Characteristics table). This can be accomplished by either DC biasing the input and AC coupling the input signal, or alternatively, by direct coupling if the output of the driving stage is also biased to half supply.

Arranged this way, the LMH6504 will respond to the current flowing through R_G. The gain control relationship will be similar to the split supply arrangement with V_G measured referenced to pin 4. Keep in mind that the circuit described above will also center the output voltage to the "virtual half supply voltage".

2) Arbitrarily Referenced Input Signal

Having a wide input voltage range on the input (pin 2) (+/-3.2V typical), the LMH6504 can be configured to control the gain on signals which are not referenced to ground (e.g. Half Supply biased circuits, etc.). We will call this node the "reference node". In such cases, the other end of R_G (the side not tied to pin 3) can be tied to this reference node so that R_G will "look at" the difference between the signal and this reference only. Keep in mind that the reference node needs to source and sink the current flowing through R_G.

Application Information

GAIN ACCURACY

Gain accuracy is defined as the actual gain compared against the theoretical gain at a certain V_G (results expressed in dB) (See Figure 43).

Theoretical gain is given by:

$$A(V/V) = K \times \frac{R_F}{R_G} \times \frac{1}{1 + e^{\left[\frac{N - V_G}{V_C}\right]}} \quad (3)$$

Where K = 0.965 (nominal) N = 0.96V & V_C = 80mV @ room temperature

For a V_G range, the value specified in the tables represents the worst case accuracy over the entire range. The "Typical" value would be the worst case difference between the "Typical gain" and the "Theoretical gain". The "Max" value would be the worst case difference between the actual gain and the "Theoretical gain" for the entire population.

GAIN MATCHING

Gain matching as the limit on gain variation at a certain V_G (expressed in dB) (see Figure 43) and is specified as "Max" only (no "Typical"). For a V_G range, the value specified represents the worst case matching over the entire range. The "Max" value would be the worst case difference between the actual gain and the typical gain for the entire population.

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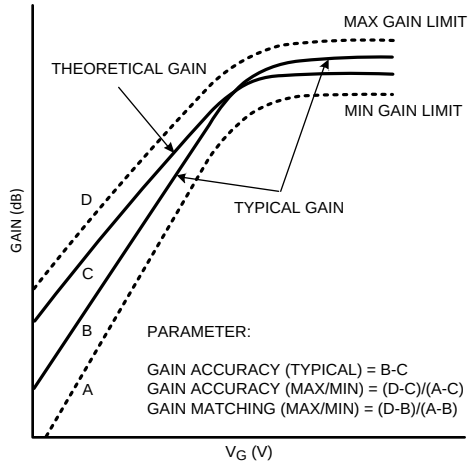


Figure 43. LMH6504 Gain Accuracy & Gain Matching Defined

GAIN PARTITIONING

If high levels of gain are needed, gain partitioning should be considered:

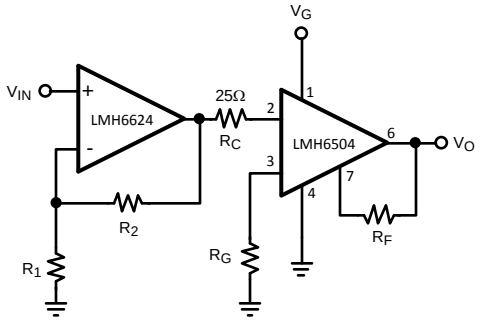


Figure 44. Gain Partitioning

The maximum gain range for this circuit is given by the following equation:

$$\text{MAXIMUM GAIN} = \left[1 + \frac{R_2}{R_1}\right] \cdot \left[\frac{R_F}{R_G}\right] \cdot K \tag{4}$$

The LMH6624 is a low noise wideband voltage feedback amplifier. Setting R_2 at 909Ω and R_1 at 100Ω produces a gain of 20 dB. Setting R_F at 1000Ω as recommended and R_G at 50Ω, produces a gain of about 26 dB in the LMH6504. The total gain of this circuit is therefore approximately 46 dB. It is important to understand that when partitioning to obtain high levels of gain, very small signal levels will drive the amplifiers to full scale output. For example, with 46 dB of gain, a 20 mV signal at the input will drive the output of the LMH6624 to 200 mV, the output of the LMH6504 to 4V. Accordingly, the designer must carefully consider the contributions of each stage to the overall characteristics. Through gain partitioning the designer is provided with an opportunity to optimize the frequency response, noise, distortion, settling time, and loading effects of each amplifier to achieve improved overall performance.

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LMH6504 GAIN CONTROL RANGE AND MINIMUM GAIN

Before discussing Gain Control Range, it is important to understand the issues which limit it. The minimum gain of the LMH6504, theoretically, is zero, but in practical circuits is limited by the amount of feedthrough, here defined as the gain when V_G = 0V. Capacitive coupling through the board and package as well as coupling through the supplies will determine the amount of feedthrough. Even at DC, the input signal will not be completely rejected. At high frequencies feedthrough will get worse because of its capacitive nature. At frequencies below 10 MHz, the feed through will be less than −60 dB and therefore, it can be said that with A_{VMAX} = 20 dB, the gain control range is 80 dB.

LMH6504 GAIN CONTROL FUNCTION

In the plot, Gain vs. V_G, we can see the gain as a function of the control voltage. The “Gain (V/V)” plot, sometimes referred to as the S-curve, is the linear (V/V) gain. This is a hyperbolic tangent relationship and is given by Equation 3. The “Gain (dB)” plots the gain in dB and is linear over a wide range of gains. Because of this, the LMH6504 gain control is referred to as “linear-in-dB.”

For applications where the LMH6504 will be used at the heart of a closed loop AGC circuit, the S-curve control characteristic provides a broad linear (in dB) control range with soft limiting at the highest gains where large changes in control voltage result in small changes in gain. For applications requiring a fully linear (in dB) control characteristic, use the LMH6504 at half gain and below ($V_G \leq$ 1V).

AVOIDING OVERDRIVE OF THE LMH6504 GAIN CONTROL INPUT

There is an additional requirement for the LMH6504 Gain Control Input (V_G): V_G must not exceed +2.3V (with ±5V supplies). The gain control circuitry may saturate and the gain may actually be reduced. In applications where V_G is being driven from a DAC, this can easily be addressed in the software. If there is a linear loop driving V_G, such as an AGC loop, other methods of limiting the input voltage should be implemented. One simple solution is to place a 2.2:1 resistive divider on the V_G input. If the device driving this divider is operating off of ±5V supplies as well, its output will not exceed 5V and through the divider V_G can not exceed 2.3V.

IMPROVING THE LMH6504 LARGE SIGNAL PERFORMANCE

Figure 45 illustrates an inverting gain scheme for the LMH6504.

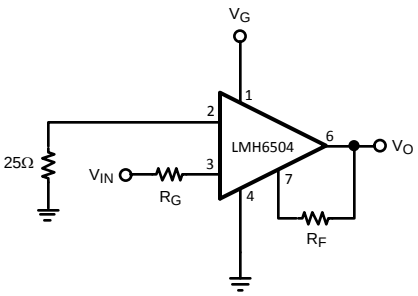


Figure 45. Inverting Amplifier

The input signal is applied through the R_G resistor. The V_{IN} pin should be grounded through a 25Ω resistor. The maximum gain range of this configuration is given in the following equation:

$$A_{VMAX} = -\left[\frac{R_F}{R_G}\right] \cdot K \quad (5)$$

The inverting slew rate of the LMH6504 is much higher than that of the non-inverting slew rate. This 2X performance improvement comes about because in the non-inverting configuration, the slew rate of the overall amplifier is limited by the input buffer. In the inverting circuit, the input buffer remains at a fixed voltage and does not affect slew rate.

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TRANSMISSION LINE MATCHING

One method for matching the characteristic impedance of a transmission line is to place the appropriate resistor at the input or output of the amplifier. Figure 46 shows a typical circuit configuration for matching transmission lines.

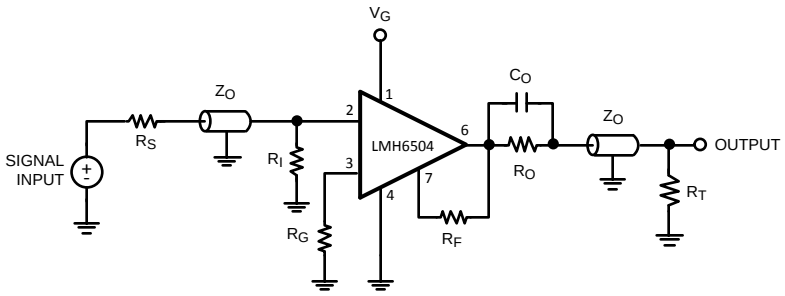


Figure 46. TRANSMISSION LINE MATCHING

The resistors R_S, R_I, R_O, and R_T are equal to the characteristic impedance, Z_O, of the transmission line or cable. Use C_O to match the output transmission line over a greater frequency range. It compensates for the increase of the op amp's output impedance with frequency.

MINIMIZING PARASITIC EFFECTS ON SMALL SIGNAL BANDWIDTH

The best way to minimize parasitic effects is to use surface mount components and to minimize lead lengths and component distance from the LMH6504. For designs utilizing through-hole components, specifically axial resistors, resistor self-capacitance should be considered. Example: the average magnitude of parasitic capacitance of RN55D 1% metal film resistors is about 0.15 pF with variations of as much as 0.1 pF between lots. Given the LMH6504's extended bandwidth, these small parasitic reactance variations can cause measurable frequency response variations in the highest octave. We therefore recommend the use of surface mount resistors to minimize these parasitic reactance effects.

RECOMMENDATIONS

Here are some recommendations to avoid problems and to get the best performance:

- Do not place a capacitor across R_F. However, an appropriately chosen series RC combination could be used to shape the frequency response.
- Keep traces connecting R_F separated and as short as possible
- Place a small resistor (20-50Ω) between the output and C_L
- Cut away the ground plane, if any, under R_G
- Keep decoupling capacitors as close as possible to the LMH6504.
- Connect pin 2 through a minimum resistance of 25Ω.

ADJUSTING OFFSETS AND DC LEVEL SHIFTING

Offsets can be broken into two parts: an input-referred term and an output-referred term. These errors can be trimmed using the circuit in Figure 47. First set V_G to 0V and adjust the trim pot R_4 to null the offset voltage at the output. This will eliminate the output stage offsets. Next set V_G to 2V and adjust the trim pot R_1 to null the offset voltage at the output. This will eliminate the input stage offsets.

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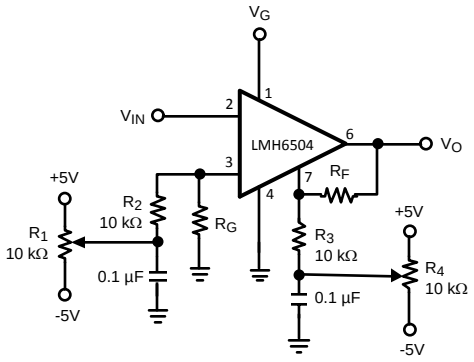


Figure 47. OFFSET ADJUST CIRCUIT

DIGITAL GAIN CONTROL

Digitally variable gain control can be easily realized by driving the LMH6504's gain control input with a digital-to-analog converter (DAC). Figure 48 illustrates such an application. This circuit employs Texas Instruments' eight-bit DAC0830, the LMC8101 MOS input op-amp (Rail-to-Rail Input/Output), and the LMH6504 VGA. With V_{REF} set to 2V, the circuit provides up to 80 dB of gain control in 256 steps with up to 0.05% full scale resolution. The maximum gain of this circuit is 20 dB.

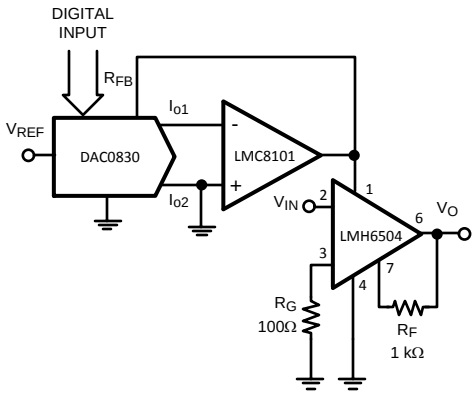


Figure 48. Digital Gain Control

USING THE LMH6504 IN AGC APPLICATIONS

In AGC applications, the control loop forces the LMH6504 to have a fixed output amplitude. The input amplitude will vary over a wide range and this can be the issue that limits dynamic range. At high input amplitudes, the distortion due to the input buffer driving R_G may exceed that which is produced by the output amplifier driving the load. In the plot, Distortion vs. Gain, total harmonic distortion (THD) is plotted over a gain range of nearly 35 dB for a fixed output amplitude of 0.25 V_{PP} in the specified configuration, R_F = 1k, R_G = 100Ω. When the gain is adjusted to -15 dB (i.e. 35 dB down from A_{VMAX}), the input amplitude would be 1.41 V_{PP} and we can see the distortion is at its worst at this gain. If the output amplitude of the AGC were to be raised above 0.25 V_{PP}, the input amplitudes for gains 40 dB down from A_{VMAX} would be even higher and the distortion would degrade further. It is for this reason that we recommend lower output amplitudes if wide gain ranges are desired. Using a post-amp like the LMH6714/ 6720/ 6722 family or LMH6702 would be the best way to preserve dynamic range and yield output amplitudes much higher than 100 mV_{PP}. Another way of addressing distortion performance and its limitations on dynamic range, would be to raise the value of R_G. Just like any other high-speed amplifier, by increasing the load resistance, and therefore decreasing the demanded load current, the distortion performance will be improved in most cases. With an increased R_G, R_F will also have to be increased to keep the same A_{VMAX} and this will decrease the overall bandwidth. It may be possible to insert a series RC combination across R_F in order to counteract the negative effect on BW when a large R_F is used.

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AUTOMATIC GAIN CONTROL (AGC) #1

Fast Response AGC Loop

The AGC circuit shown in Figure 49 will correct a 6 dB input amplitude step in 100 ns. The circuit includes a two op-amp precision rectifier amplitude detector (U1 and U2), and an integrator (U3) to provide high loop gain at low frequencies. The output amplitude is set by R_9. Some notes on building fast AGC loops: Precision rectifiers work best with large output signals. Accuracy is improved by blocking DC offsets, as shown in Figure 49.

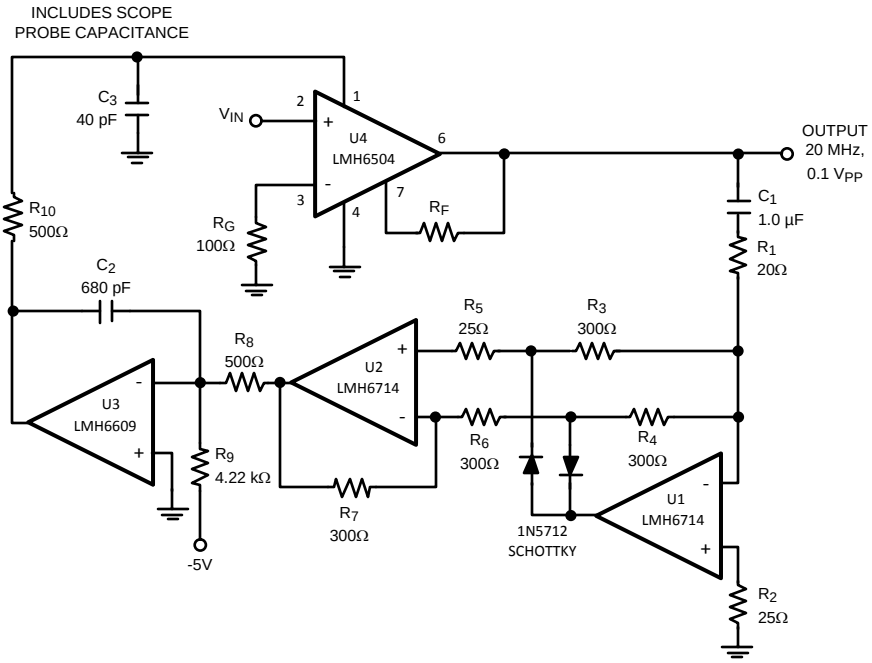


Figure 49. Automatic Gain Control Circuit #1

Signal frequencies must not reach the gain control port of the LMH6504, or the output signal will be distorted (modulated by itself). A fast settling AGC needs additional filtering beyond the integrator stage to block signal frequencies. This is provided in Figure 49 by a simple R-C filter (R_{10} and C_3); better distortion performance can be achieved with a more complex filter. These filters should be scaled with the input signal frequency. Loops with slower response time (longer integration time constants) may not need the $R_{10} – C_3$ filter.

Checking the loop stability can be done by monitoring the V_G voltage while applying a step change in input signal amplitude. Changing the input signal amplitude can be easily done with an arbitrary waveform generator.

AUTOMATIC GAIN CONTROL (AGC) #2

Figure 50 illustrates an automatic gain control circuit that employs two LMH6504's. In this circuit, U1 receives the input signal and produces an output signal of constant amplitude. U2 is configured to provide negative feedback. U2 generates a rectified gain control signal that works against an adjustable bias level which may be set by the potentiometer and R_B. C_I integrates the bias and negative feedback. The resultant gain control signal is applied to the U1 gain control input V_G. The bias adjustment allows the U1 output to be set at an arbitrary level less than the maximum output specification of the amplifier. Rectification is accomplished in U2 by driving both the amplifier input and the gain control input with the U1 output signal. The voltage divider that is formed by R_1 and R_2, sets the rectifier gain.

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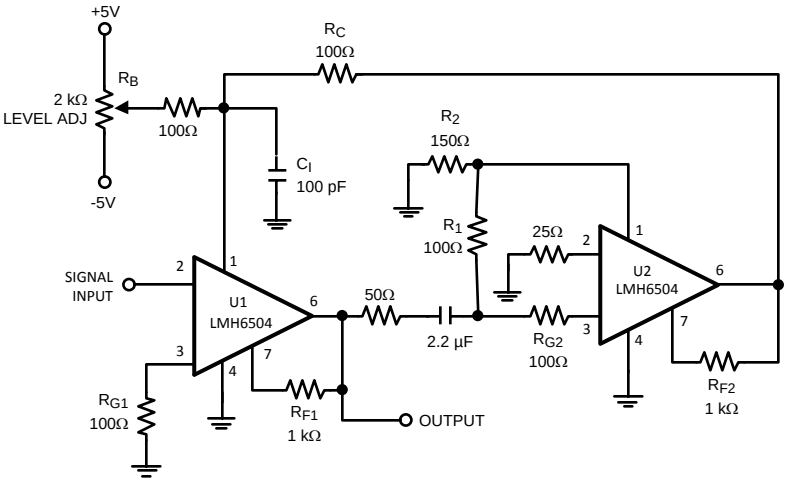


Figure 50. Automatic Gain Control Circuit #2

CIRCUIT LAYOUT CONSIDERATIONS & EVALUATION BOARD

A good high frequency PCB layout including ground plane construction and power supply bypassing close to the package are critical to achieving full performance. The amplifier is sensitive to stray capacitance to ground at the I¯input (pin 7); keep node trace area small. Shunt capacitance across the feedback resistor should not be used to compensate for this effect. Capacitance to ground should be minimized by removing the ground plane from under the body of R_G. Parasitic or load capacitance directly on the output (pin 6) degrades phase margin leading to frequency response peaking.

The LMH6504 is fully stable when driving a 100Ω load. With reduced load (e.g. 1k.) there is a possibility of instability at very high frequencies beyond 400 MHz especially with a capacitive load. When the LMH6504 is connected to a light load as such, it is recommended to add a snubber network to the output (e.g. 100Ω and 39 pF in series tied between the LMH6504 output and ground). C_L can also be isolated from the output by placing a small resistor in series with the output (pin 6).

Component parasitics also influence high frequency results. Therefore it is recommended to use metal film resistors such as RN55D or leadless components such as surface mount devices. High profile sockets are not recommended.

Texas Instruments suggests the following evaluation board as a guide for high frequency layout and as an aid in device testing and characterization:

Device	Package	Evaluation Board Part Number
LMH6504	SOIC	CLC730066

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REVISION HISTORY

Changes from Revision C (March 2013) to Revision D **Page**

- Changed layout of National Data Sheet to TI format 20

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PACKAGING INFORMATION

Orderable part number	Status (1)	Material type (2)	Package | Pins	Package qty | Carrier	RoHS (3)	Lead finish/ Ball material (4)	MSL rating/ Peak reflow (5)	Op temp (°C)	Part marking (6)
LMH6504MA/NOPB	NRND	Production	SOIC (D) | 8	95 | TUBE	Yes	SN	Level-1-260C-UNLIM	-40 to 85	LMH65 04MA
LMH6504MA/NOPB.A	NRND	Production	SOIC (D) | 8	95 | TUBE	Yes	SN	Level-1-260C-UNLIM	-40 to 85	LMH65 04MA
LMH6504MAX/NOPB	NRND	Production	SOIC (D) | 8	2500 | LARGE T&R	Yes	SN	Level-1-260C-UNLIM	-40 to 85	LMH65 04MA
LMH6504MAX/NOPB.A	NRND	Production	SOIC (D) | 8	2500 | LARGE T&R	Yes	SN	Level-1-260C-UNLIM	-40 to 85	LMH65 04MA
LMH6504MM/NOPB	NRND	Production	VSSOP (DGK) | 8	1000 | SMALL T&R	Yes	SN	Level-1-260C-UNLIM	-40 to 85	A93A
LMH6504MM/NOPB.A	NRND	Production	VSSOP (DGK) | 8	1000 | SMALL T&R	Yes	SN	Level-1-260C-UNLIM	-40 to 85	A93A

(1) **Status:** For more details on status, see our product life cycle.

(2) **Material type:** When designated, preproduction parts are prototypes/experimental devices, and are not yet approved or released for full production. Testing and final process, including without limitation quality assurance, reliability performance testing, and/or process qualification, may not yet be complete, and this item is subject to further changes or possible discontinuation. If available for ordering, purchases will be subject to an additional waiver at checkout, and are intended for early internal evaluation purposes only. These items are sold without warranties of any kind.

(3) **RoHS values:** Yes, No, RoHS Exempt. See the TI RoHS Statement for additional information and value definition.

(4) **Lead finish/Ball material:** Parts may have multiple material finish options. Finish options are separated by a vertical ruled line. Lead finish/Ball material values may wrap to two lines if the finish value exceeds the maximum column width.

(5) **MSL rating/Peak reflow:** The moisture sensitivity level ratings and peak solder (reflow) temperatures. In the event that a part has multiple moisture sensitivity ratings, only the lowest level per JEDEC standards is shown. Refer to the shipping label for the actual reflow temperature that will be used to mount the part to the printed circuit board.

(6) **Part marking:** There may be an additional marking, which relates to the logo, the lot trace code information, or the environmental category of the part.

Multiple part markings will be inside parentheses. Only one part marking contained in parentheses and separated by a "~" will appear on a part. If a line is indented then it is a continuation of the previous line and the two combined represent the entire part marking for that device.

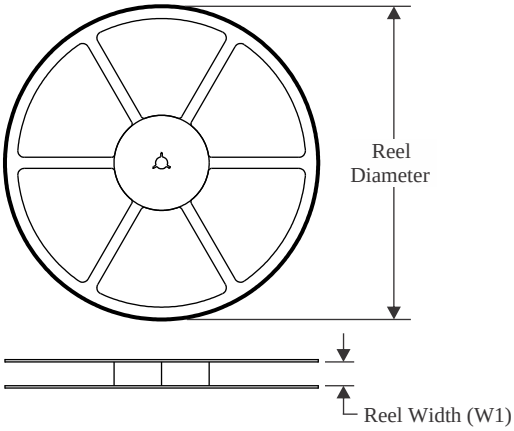
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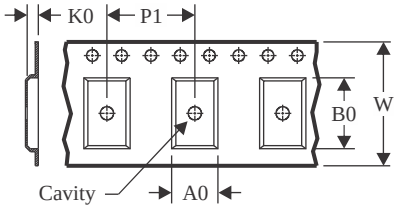
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TAPE AND REEL INFORMATION

REEL DIMENSIONS

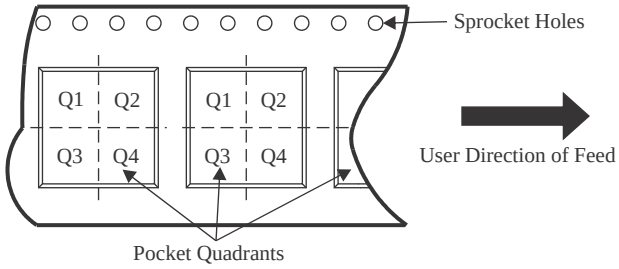


TAPE DIMENSIONS



A0	Dimension designed to accommodate the component width
B0	Dimension designed to accommodate the component length
K0	Dimension designed to accommodate the component thickness
W	Overall width of the carrier tape
P1	Pitch between successive cavity centers

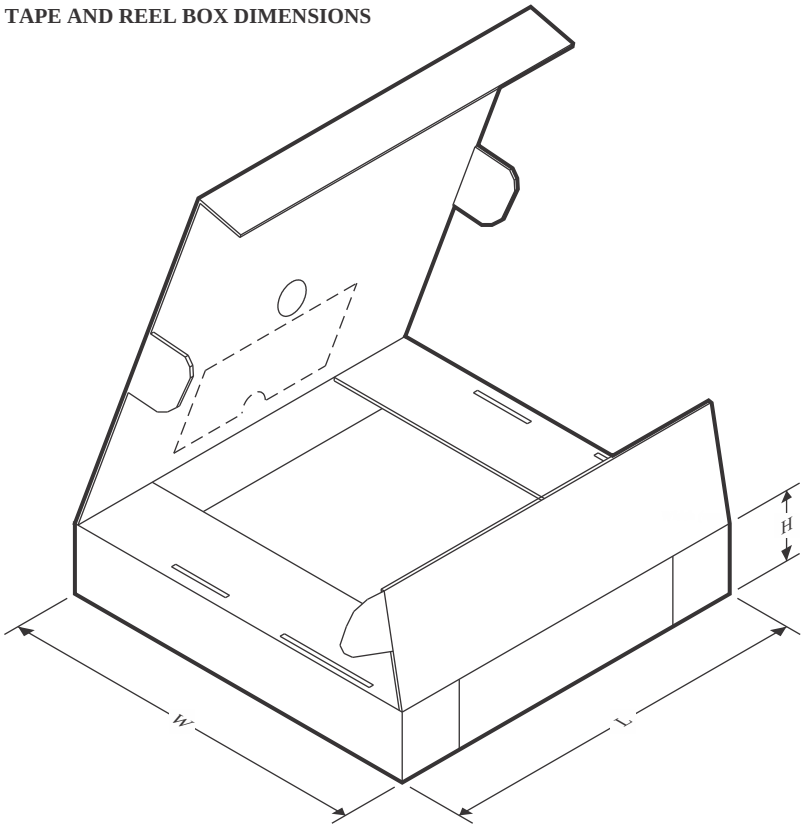
QUADRANT ASSIGNMENTS FOR PIN 1 ORIENTATION IN TAPE



*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Reel Diameter (mm)	Reel Width W1 (mm)	A0 (mm)	B0 (mm)	K0 (mm)	P1 (mm)	W (mm)	Pin1 Quadrant
LMH6504MAX/NOPB	SOIC	D	8	2500	330.0	12.4	6.4	5.2	2.1	8.0	12.0	Q1
LMH6504MM/NOPB	VSSOP	DGK	8	1000	177.8	12.4	5.3	3.4	1.4	8.0	12.0	Q1

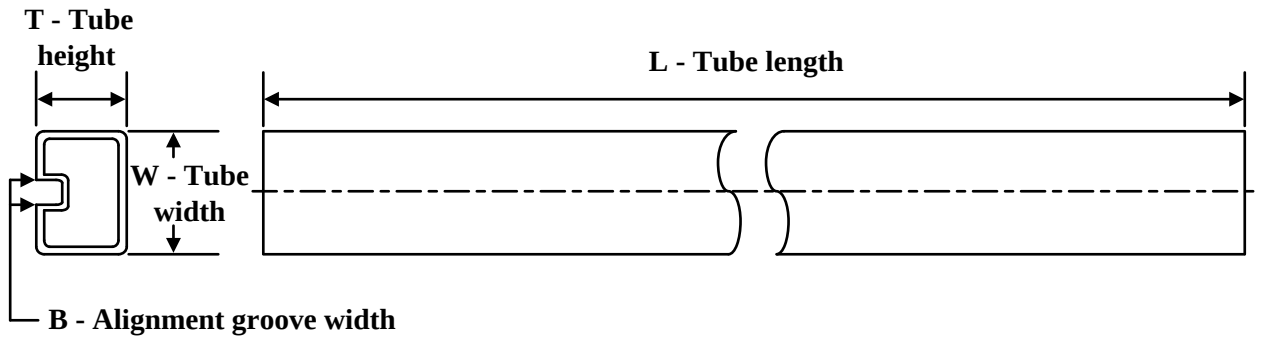
TAPE AND REEL BOX DIMENSIONS



*All dimensions are nominal

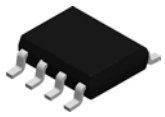
Device	Package Type	Package Drawing	Pins	SPQ	Length (mm)	Width (mm)	Height (mm)
LMH6504MAX/NOPB	SOIC	D	8	2500	367.0	367.0	35.0
LMH6504MM/NOPB	VSSOP	DGK	8	1000	208.0	191.0	35.0

TUBE



*All dimensions are nominal

Device	Package Name	Package Type	Pins	SPQ	L (mm)	W (mm)	T (µm)	B (mm)
LMH6504MA/NOPB	D	SOIC	8	95	495	8	4064	3.05
LMH6504MA/NOPB.A	D	SOIC	8	95	495	8	4064	3.05

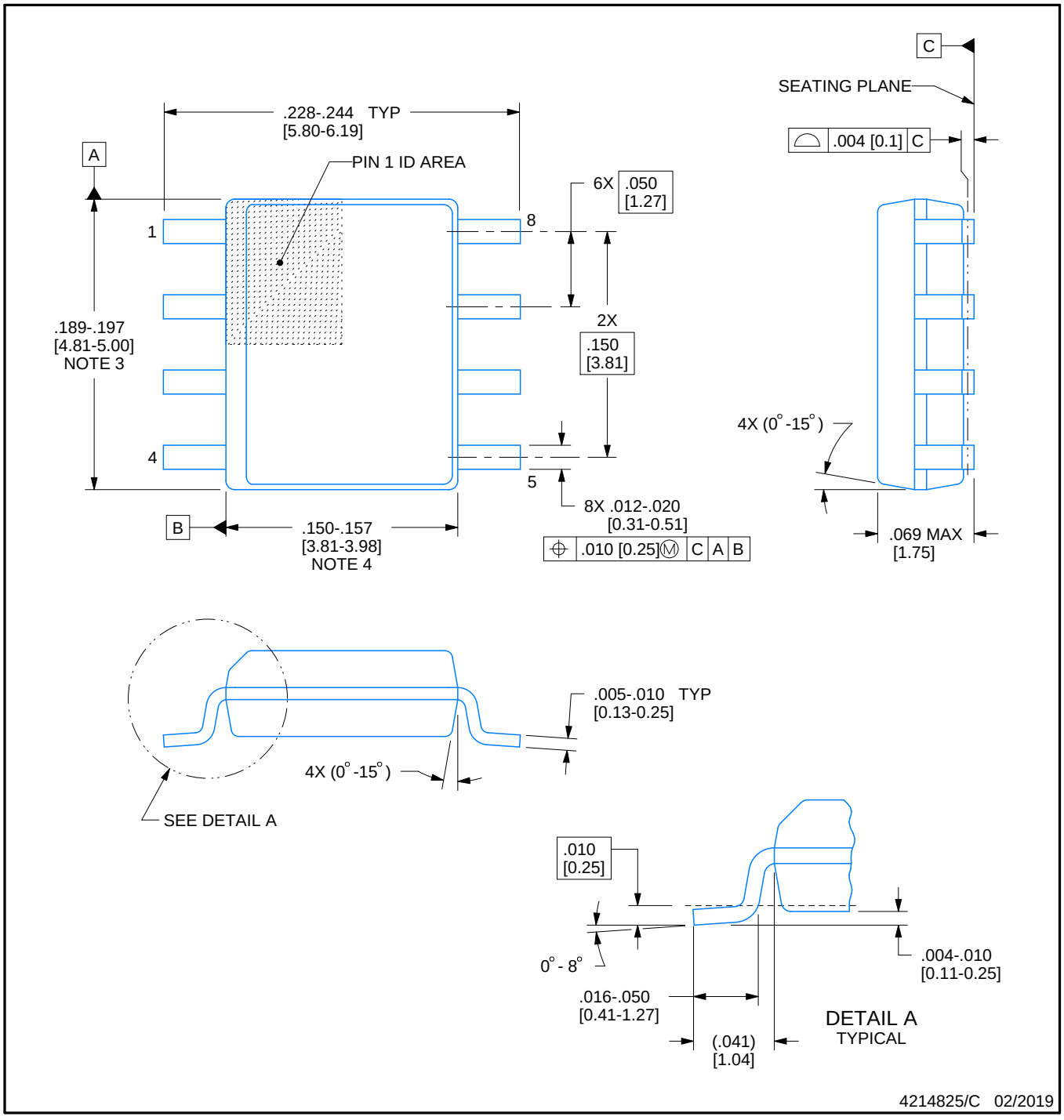


PACKAGE OUTLINE

D0008A

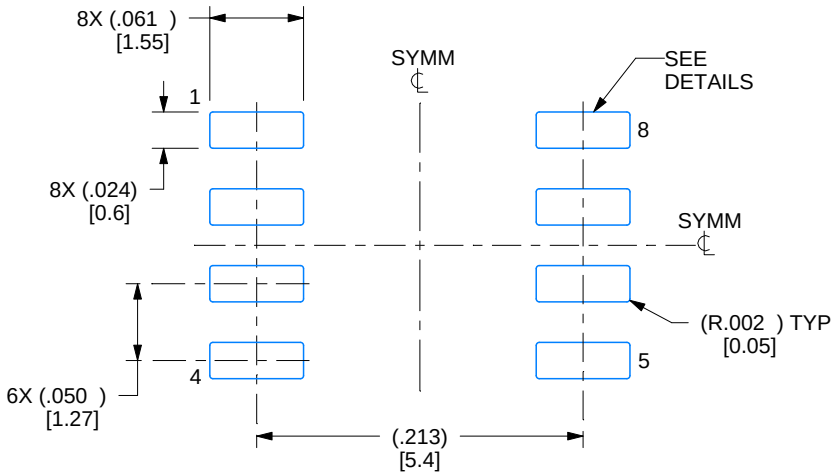
SOIC - 1.75 mm max height

SMALL OUTLINE INTEGRATED CIRCUIT

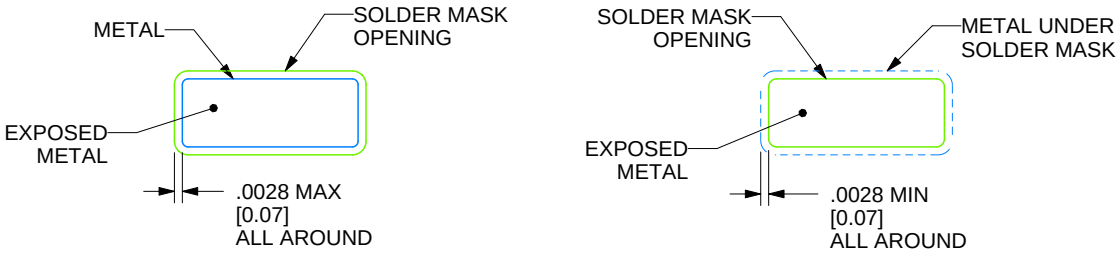


NOTES:

1. Linear dimensions are in inches [millimeters]. Dimensions in parenthesis are for reference only. Controlling dimensions are in inches. Dimensioning and tolerancing per ASME Y14.5M.
2. This drawing is subject to change without notice.
3. This dimension does not include mold flash, protrusions, or gate burrs. Mold flash, protrusions, or gate burrs shall not exceed .006 [0.15] per side.
4. This dimension does not include interlead flash.
5. Reference JEDEC registration MS-012, variation AA.



LAND PATTERN EXAMPLE
EXPOSED METAL SHOWN
SCALE:8X



SOLDER MASK DETAILS

4214825/C 02/2019

NOTES: (continued)

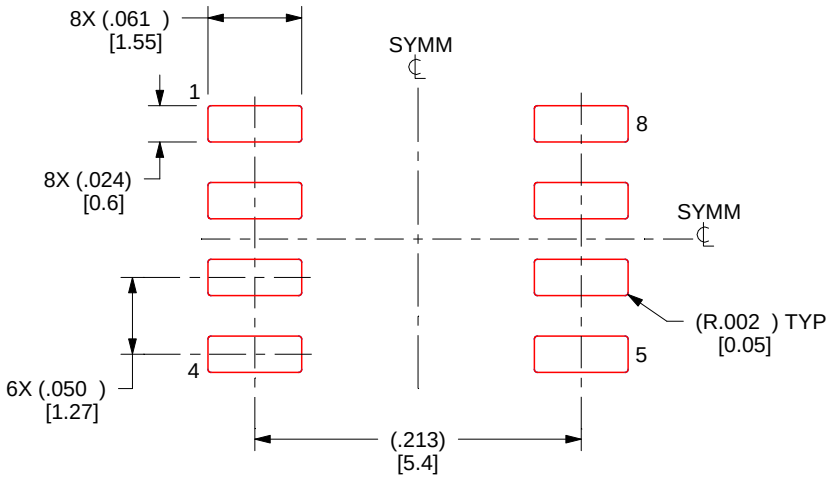
6. Publication IPC-7351 may have alternate designs.
7. Solder mask tolerances between and around signal pads can vary based on board fabrication site.

EXAMPLE STENCIL DESIGN

D0008A

SOIC - 1.75 mm max height

SMALL OUTLINE INTEGRATED CIRCUIT



SOLDER PASTE EXAMPLE
BASED ON .005 INCH [0.125 MM] THICK STENCIL
SCALE:8X

4214825/C 02/2019

NOTES: (continued)

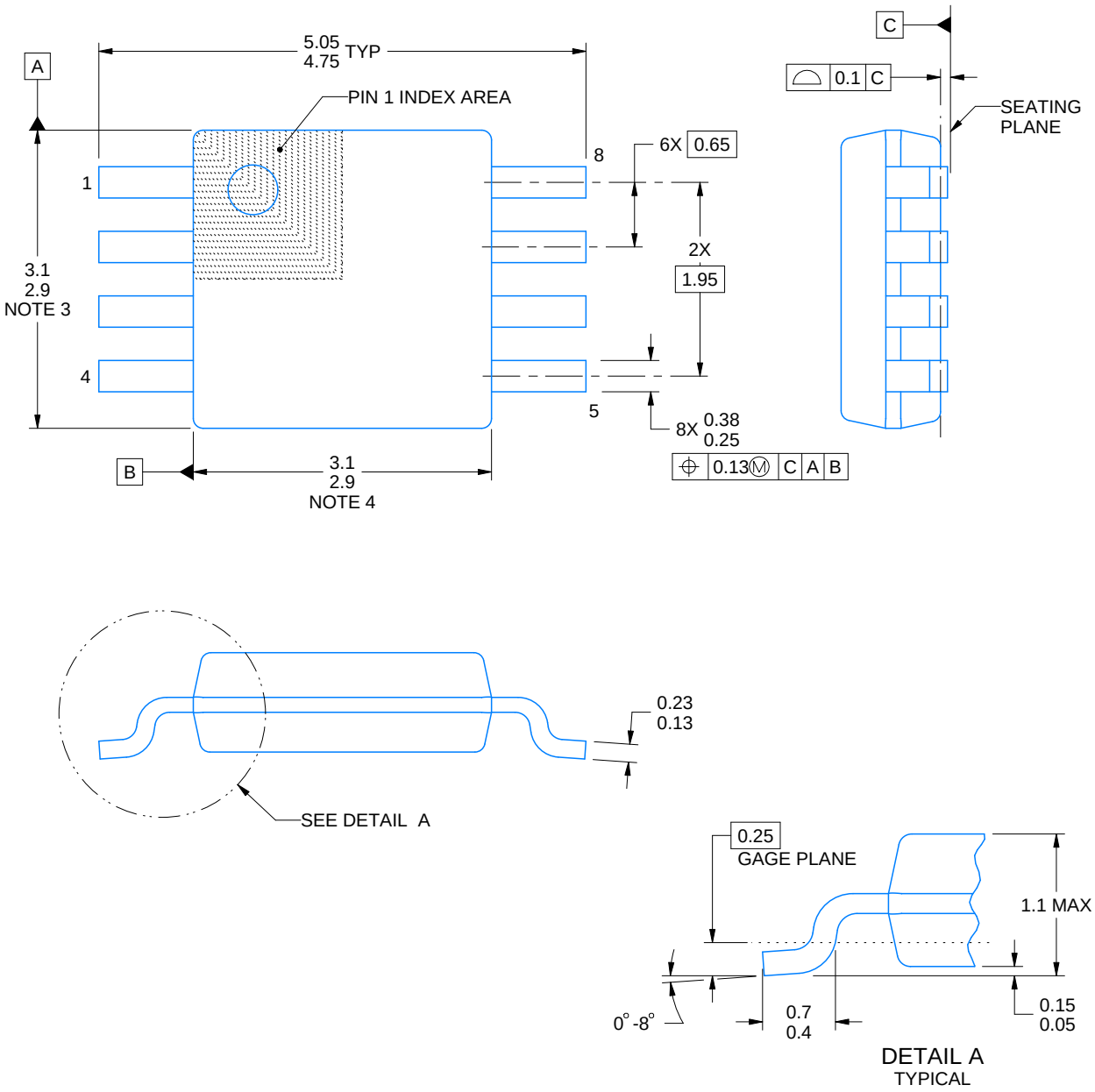
8. Laser cutting apertures with trapezoidal walls and rounded corners may offer better paste release. IPC-7525 may have alternate design recommendations.
9. Board assembly site may have different recommendations for stencil design.

PACKAGE OUTLINE

DGK0008A

VSSOP - 1.1 mm max height

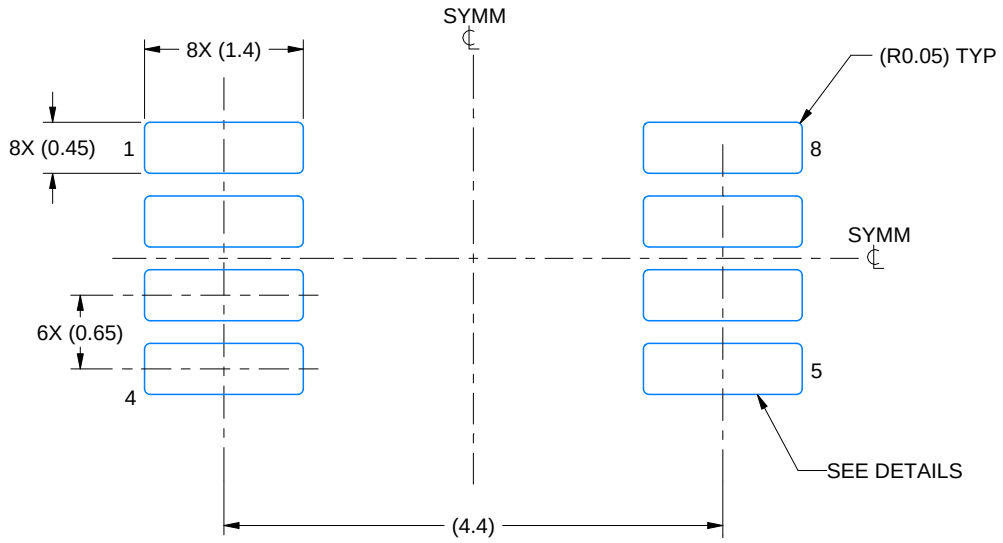
SMALL OUTLINE PACKAGE



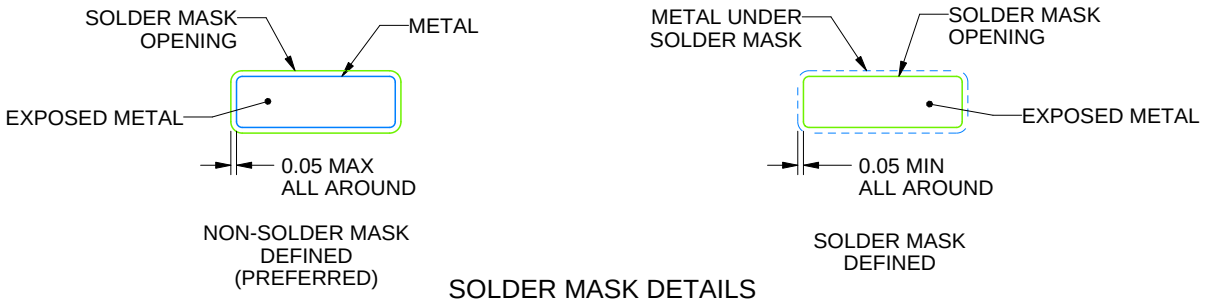
PowerPAD is a trademark of Texas Instruments.

NOTES:

1. All linear dimensions are in millimeters. Any dimensions in parenthesis are for reference only. Dimensioning and tolerancing per ASME Y14.5M.
2. This drawing is subject to change without notice.
3. This dimension does not include mold flash, protrusions, or gate burrs. Mold flash, protrusions, or gate burrs shall not exceed 0.15 mm per side.
4. This dimension does not include interlead flash. Interlead flash shall not exceed 0.25 mm per side.
5. Reference JEDEC registration MO-187.



LAND PATTERN EXAMPLE
EXPOSED METAL SHOWN
SCALE: 15X

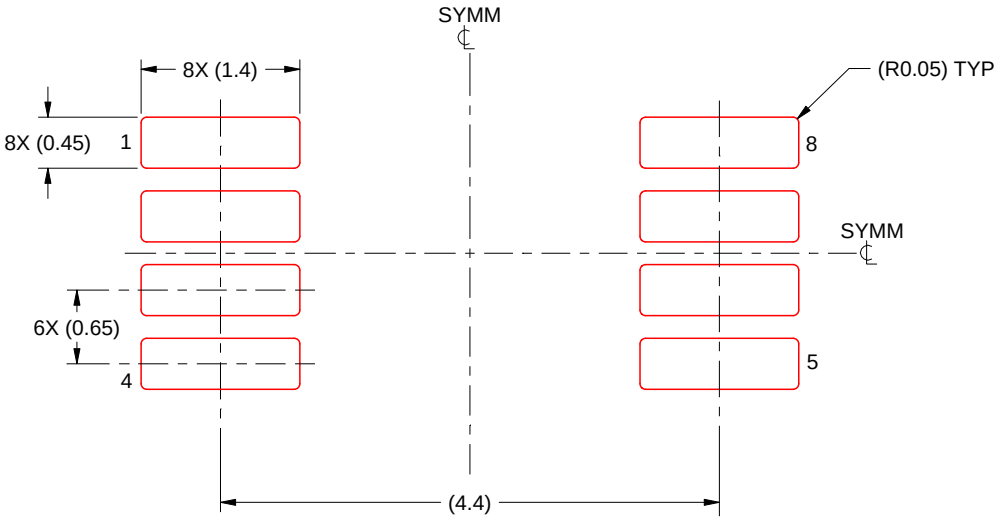


SOLDER MASK DETAILS

4214862/A 04/2023

NOTES: (continued)

6. Publication IPC-7351 may have alternate designs.
7. Solder mask tolerances between and around signal pads can vary based on board fabrication site.
8. Vias are optional depending on application, refer to device data sheet. If any vias are implemented, refer to their locations shown on this view. It is recommended that vias under paste be filled, plugged or tented.
9. Size of metal pad may vary due to creepage requirement.



SOLDER PASTE EXAMPLE
SCALE: 15X

4214862/A 04/2023

NOTES: (continued)

11. Laser cutting apertures with trapezoidal walls and rounded corners may offer better paste release. IPC-7525 may have alternate design recommendations.
12. Board assembly site may have different recommendations for stencil design.

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