

3.5V 至 28V 输入电压, 1.7A 输出电流, 带有集成金属氧化物半导体场效应晶体管 (MOSFET) 的非同步降压稳压器

查询样品: [TPS5402](#)

特性

- 3.5V 至 28V 的宽输入电压范围
- 高达 1.7A 的最大持续输出负载电流
- 脉冲跳跃模式可在轻负载时实现高效率
- 高轻负载效率
- 频率展频以减少电磁干扰 (EMI)
- 由一个外部电阻器设定 50kHz 至 1.1MHz 的可调开关频率
(将引脚 **ROSC** 悬空。将频率设定在 120kHz 并且接地连接至 70kHz)
- 频率展频以缓解 EMI 问题
- 峰值电流模式控制
- 逐周期过流保护
- 外部软启动
- 采用小外形集成电路 (SOIC)8 封装

应用范围

- 5V, 9V, 12V 和 24V 分布式电源系统
- 消费类应用, 诸如家用电器、机顶盒、CPE 设备、LCD 显示器、外设、和电池充电器
- 工业用和车载娱乐系统电源

说明

TPS5402 是一款具有宽运行输入电压范围 (3.5V 至 28V) 的单片非同步降压稳压器。此器件执行内部斜坡补偿的电流模式控制来减少组件数量。

TPS5402 还特有一个轻负载脉冲跳跃模式, 此特性可在轻负载时减少为系统供电的输入电源的功率损失。

可使用一个外部电阻器将此转换器的开关频率设定在 50kHz 至 1.1MHz 之间。引入了频率展频操作以减少 EMI。

具有频率折返功能的逐周期电流限制在过载情况下保护集成电路 (IC)。



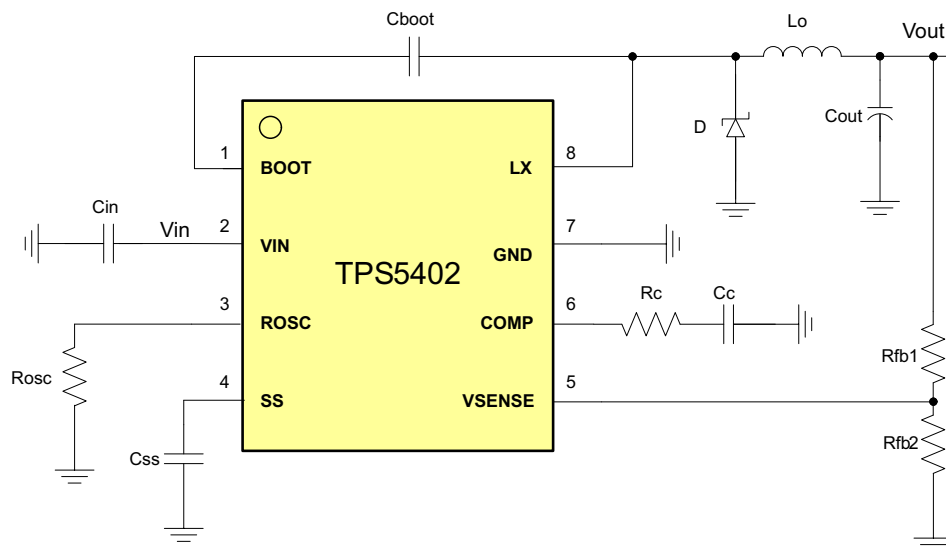
Please be aware that an important notice concerning availability, standard warranty, and use in critical applications of Texas Instruments semiconductor products and disclaimers thereto appears at the end of this data sheet.



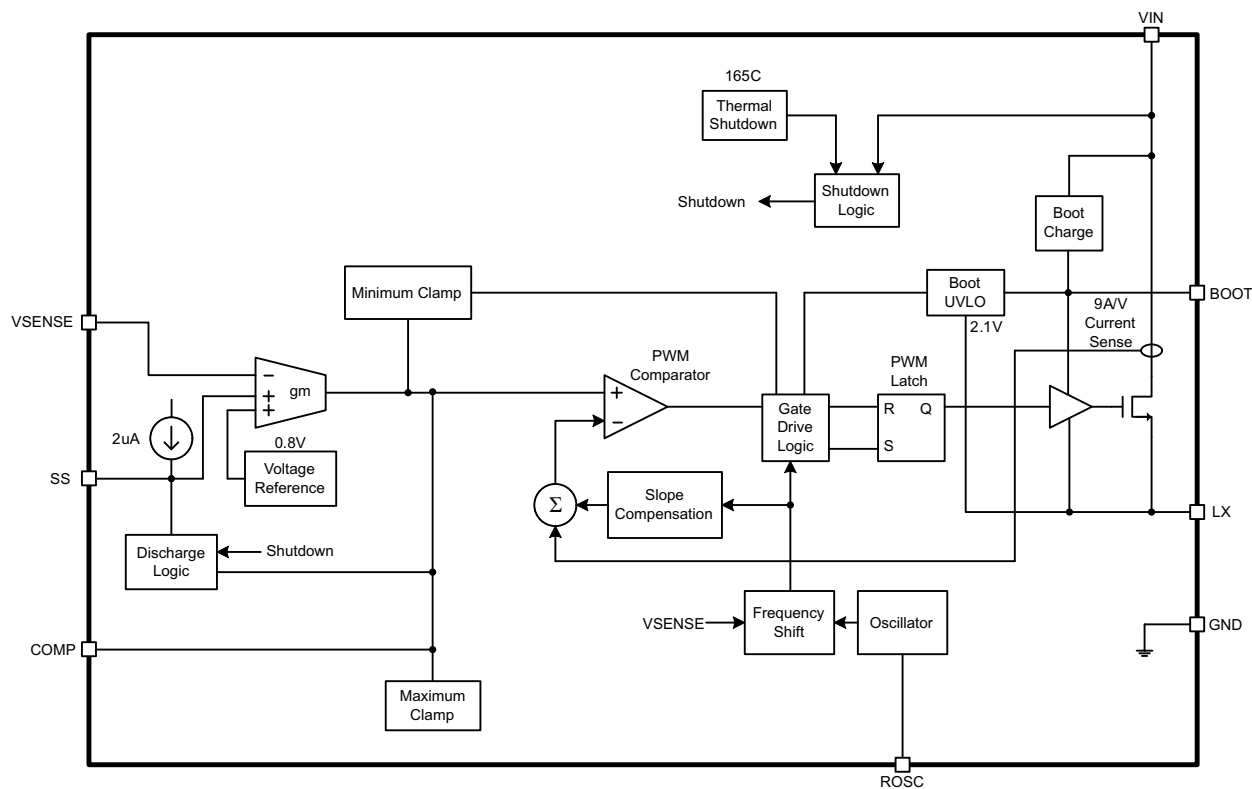
This integrated circuit can be damaged by ESD. Texas Instruments recommends that all integrated circuits be handled with appropriate precautions. Failure to observe proper handling and installation procedures can cause damage.

ESD damage can range from subtle performance degradation to complete device failure. Precision integrated circuits may be more susceptible to damage because very small parametric changes could cause the device not to meet its published specifications.

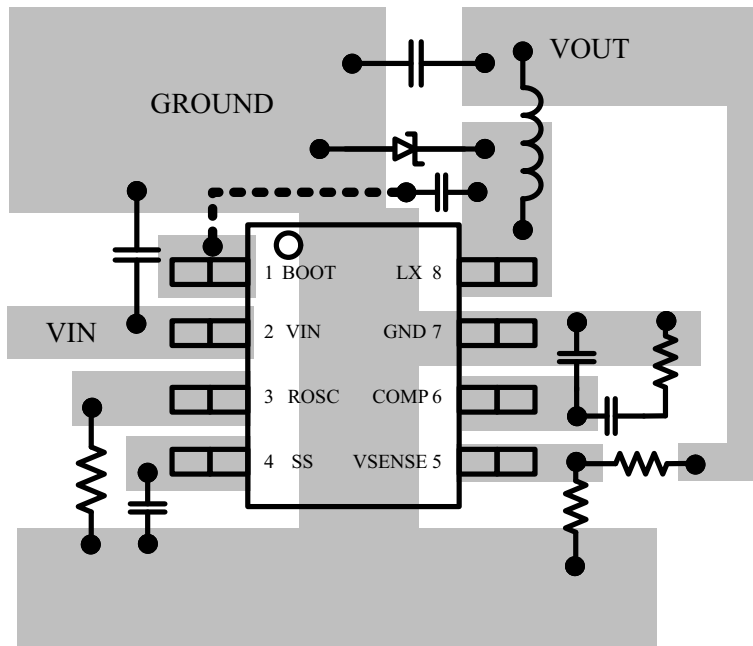
TYPICAL APPLICATION



FUNCTIONAL BLOCK DIAGRAM



PCB LAYOUT

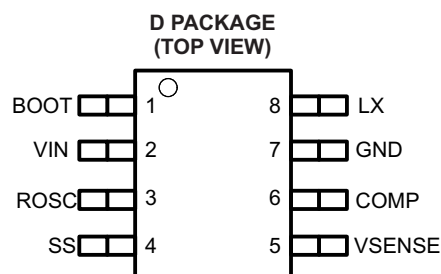


ORDERING INFORMATION⁽¹⁾

T _A	PACKAGE ⁽²⁾	ORDERABLE PART NUMBER	TOP-SIDE MARKING
–40°C to 85°C	8-pin SOIC (D)	TPS5402DR	TPS5402

- (1) For the most current package and ordering information, see the Package Option Addendum at the end of this document, or see the TI web site at www.ti.com.
- (2) Package drawings, thermal data, and symbolization are available at www.ti.com/packaging.

PIN OUT



TERMINAL FUNCTIONS

NAME	NO.	DESCRIPTION
BOOT	1	A 0.1-μF bootstrap capacitor is required between BOOT and LX.
VIN	2	Input supply voltage, 3.5 V to 28 V
ROSC	3	Switching frequency program pin. Connect a resistor to this pin to set the switching frequency. Connect the pin to ground for a default 70-kHz switching frequency. Leave the pin open for 120-kHz switching frequency.
SS	4	Soft start pin. An external capacitor connected to this pin sets the output rise time.
VSENSE	5	Output voltage feedback pin
COMP	6	Error amplifier output and input to the PWM comparator. Connect frequency compensation components to this pin.
GND	7	Ground
LX	8	Switching node to external inductor

ABSOLUTE MAXIMUM RATINGS ⁽¹⁾

over operating free-air temperature range (unless otherwise noted)

	Voltage range at VIN, LX	–0.3 to 30	V
	Voltage range at LX (maximum withstand voltage transient < 20 ns)	–5 to 30	V
	Voltage from BOOT to LX	–0.3 to 7	V
	Voltage at VSENSE	–0.3 to 7	V
	Voltage at SS	–0.3 to 3	V
	Voltage at ROSC	–0.3 to 3	V
	Voltage at COMP	–0.3 to 3	V
	Voltage at GND	–0.3 to 0.3	V
T _J	Operating junction temperature range	–40 to 125	°C
T _{STG}	Storage temperature range	–55 to 150	°C

- (1) Stresses beyond those listed under "absolute maximum ratings" may cause permanent damage to the device. These are stress ratings only, and functional operation of the device at these or any other conditions beyond those indicated under "recommended operating conditions" is not implied. Exposure to absolute–maximum–rated conditions for extended periods may affect device reliability.

RECOMMENDED OPERATING CONDITIONS

over operating free-air temperature range (unless otherwise noted)

	MIN	NOM	MAX	UNIT
VIN Input operating voltage	3.5		28	V
T _A Ambient temperature	–40		85	°C

THERMAL INFORMATION

THERMAL METRIC ⁽¹⁾		TPS5402	UNITS
		D	
		8 PINS	
θ _{JA}	Junction-to-ambient thermal resistance ⁽²⁾	116.7	°C/W
θ _{JCTop}	Junction-to-case (top) thermal resistance ⁽³⁾	62.4	
θ _{JB}	Junction-to-board thermal resistance ⁽⁴⁾	57.0	
ψ _{JT}	Junction-to-top characterization parameter ⁽⁵⁾	14.5	
ψ _{JB}	Junction-to-board characterization parameter ⁽⁶⁾	56.5	
θ _{JCbot}	Junction-to-case (bottom) thermal resistance ⁽⁷⁾	N/A	

- (1) 有关传统和新的热 度量的更多信息，请参阅/C 封装热度量应用报告， [SPRA953](#)。
- (2) 在 JESD51-2a 描述的环境中，按照 JESD51-7 的指定，在一个 JEDEC 标准高 K 电路板上进行仿真，从而获得自然 对流条件下的结至环境热阻。
- (3) 通过在封装顶部模拟一个冷板测试来获得结至芯片外壳（顶部）的热阻。不存在特定的 JEDEC 标准测试，但 可在 ANSI SEMI 标准 G30-88 中找到内容接近的说明。
- (4) 按照 JESD51-8 中的说明，通过 在配有用于控制 PCB 温度的环形冷板夹具的环境中进行仿真，以获得结板热阻。
- (5) 结至顶部特征参数， ψ_{JT}，估算真实系统中器件的结温，并使用 JESD51-2a（第 6 章和第 7 章）中 描述的程序从仿真数据中 提取出该参数以便获得 θ_{JA}。
- (6) 结至电路板特征参数， ψ_{JB}，估算真实系统中器件的结温，并使用 JESD51-2a（第 6 章和第 7 章）中 描述的程序从仿真数据中 提取出该参数以便获得 θ_{JA}。
- (7) 通过在外露（电源）焊盘上进行冷板测试仿真来获得 结至芯片外壳（底部）热阻。不存在特定的 JEDEC 标准 测试，但可在 ANSI SEMI 标准 G30-88 中找到内容接近的说明。

ELECTRICAL CHARACTERISTICS

 $T_A = -40^{\circ}\text{C}$ to 125°C , $V_{IN} = 12\text{ V}$ (unless otherwise noted)

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
INPUT SUPPLY						
V _{IN}	Input Voltage range		3.5		28	V
IDD _{Q_nsw}	Non switching quiescent power supply current	V _{SENSE} > 0.9 V		100		μA
UVLO	V _{IN} under voltage lockout	Rising V _{IN}		3.5		V
		Hysteresis		200		mV
FEEDBACK AND ERROR AMPLIFIER						
V _{SENSE}	Regulated output voltage	V _{IN} = 12 V	0.776	0.8	0.824	V
G _{m_EA}	Error amplifier trans-conductance	-2 μA < I _{COMP} < 2 μA, V _{COMP} = 1 V		92		μs
I _{gm}	Error amplifier source/sink current	V _{COMP} = 1 V, 100 mV overdrive		±7		μA
G _{m_SRC}	COMP voltage to inductor current Gm	V _{IN} = 12 V		9		A/V
PFM MODE AND SOFT-START						
I _{th}	Pulse skipping mode switch current threshold			300		mA
I _{SS}	Charge current			2		μA
OSCILLATOR						
f _{SW_BK}	Switching frequency range	Set by external resistor ROSC	50		1100	kHz
f _{SW}	Programmable frequency	ROSC = GND		70		kHz
		ROSC = OPEN		120		
		ROSC = 85.5 kΩ		300		
f _{jitter}	Frequency spread spectrum in percentage of f _{SW}	V _{IN} = 12 V		±6		%
f _{swing}	Jittering swing frequency in percentage of f _{SW}	V _{IN} = 12 V		1/512		
t _{min_on}	Minimum on time	V _{IN} = 12 V, T _A = 25°C		200		ns
D _{max}	Maximum duty ratio	V _{IN} = 12 V		93		%
CURRENT LIMIT						
I _{LIMIT}	Peak inductor current limit	V _{IN} = 12 V	2.2	2.5	3.1	A
MOSFET ON-RESISTANCE						
R _{dson_HS}	On resistance of high side FET	V _{IN} = 12 V		120	240	mΩ
THERMAL SHUTDOWN						
T _{TRIP}	Thermal protection trip point	Rising temperature		165		°C

TYPICAL CHARACTERISTICS

$T_A = 25^\circ\text{C}$, $V_{IN} = 12\text{ V}$, $V_{OUT} = 3.3\text{ V}$, $f_{SW} = 120\text{ kHz}$ (unless otherwise noted)

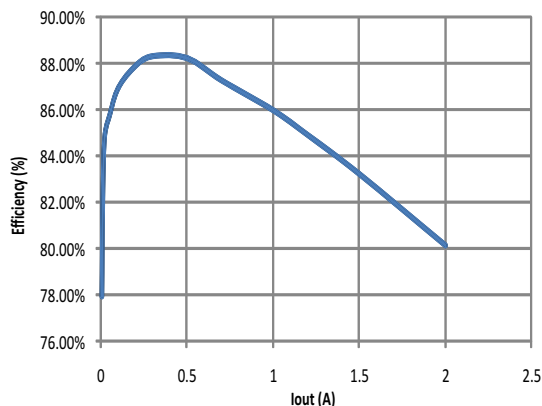


Figure 1. Efficiency
 $V_{IN} = 12\text{ V}$, $V_{OUT} = 3.3\text{ V}$

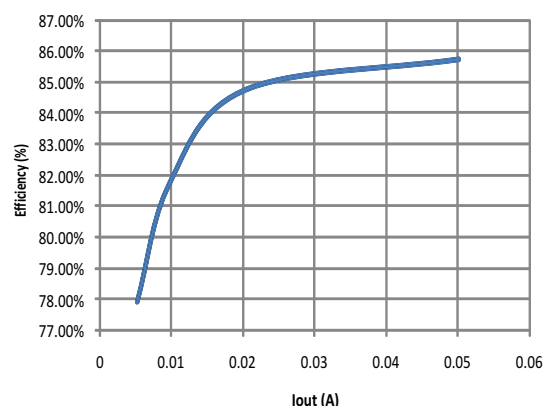


Figure 2. Efficiency
 $V_{IN} = 12\text{ V}$, $V_{OUT} = 3.3\text{ V}$

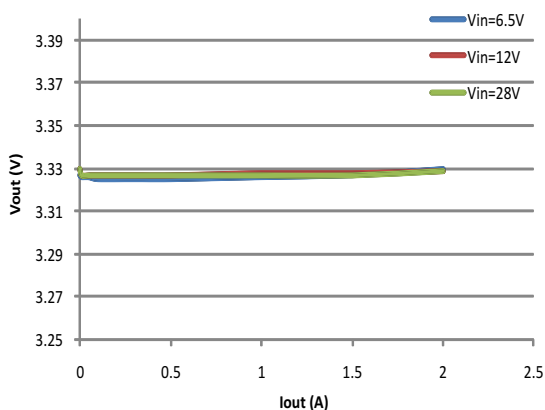


Figure 3. Load Regulation
 $V_{IN} = 12\text{ V}$, $V_{OUT} = 3.3\text{ V}$

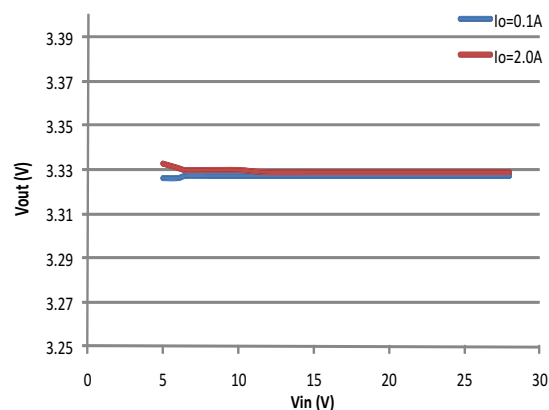


Figure 4. Line Regulation
 $V_{OUT} = 3.3\text{ V}$

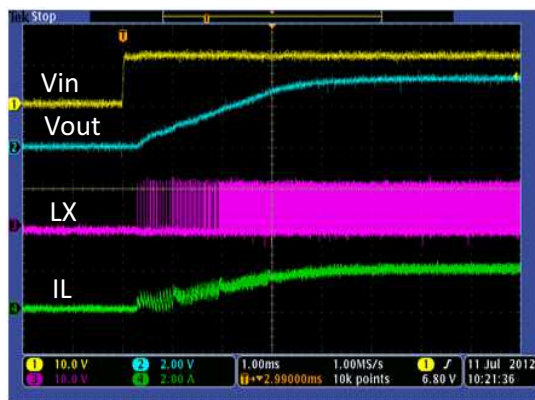


Figure 5. Startup
2-A Preset Loading

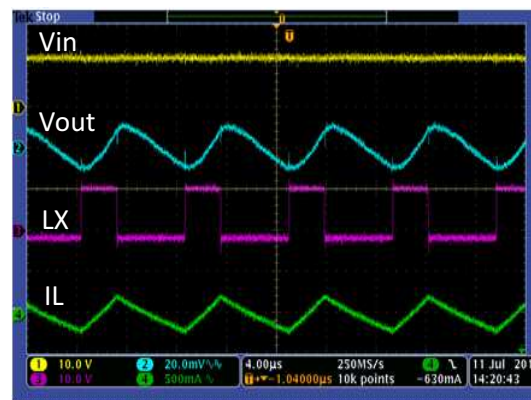


Figure 6. Steady State
 $I_O = 2\text{ A}$

TYPICAL CHARACTERISTICS (continued)

$T_A = 25^\circ\text{C}$, $V_{IN} = 12\text{ V}$, $V_{OUT} = 3.3\text{ V}$, $f_{SW} = 120\text{ kHz}$ (unless otherwise noted)

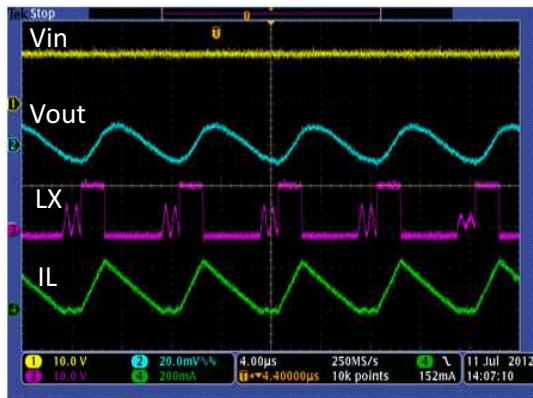


Figure 7. Steady State
 $I_O = 100\text{ mA}$

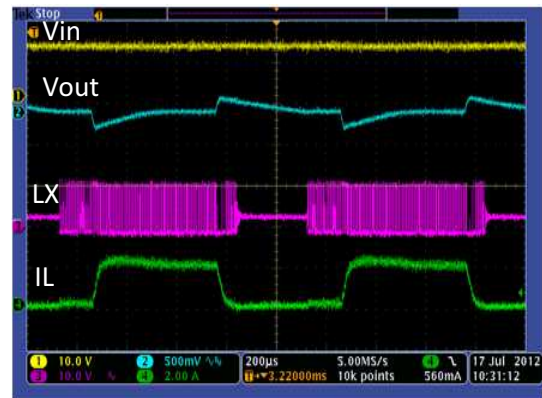


Figure 8. Load Transient
 $I_O = 0.1\text{ A to }2\text{ A}$

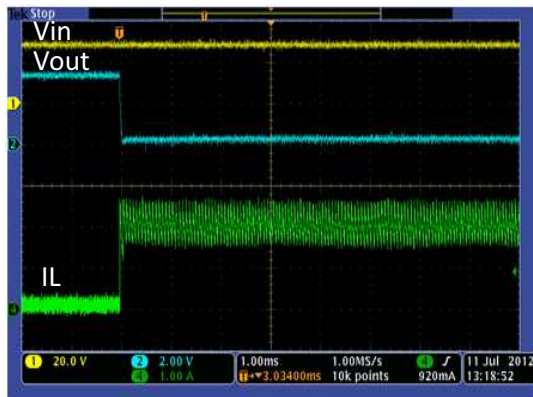


Figure 9. Short Circuit Protection

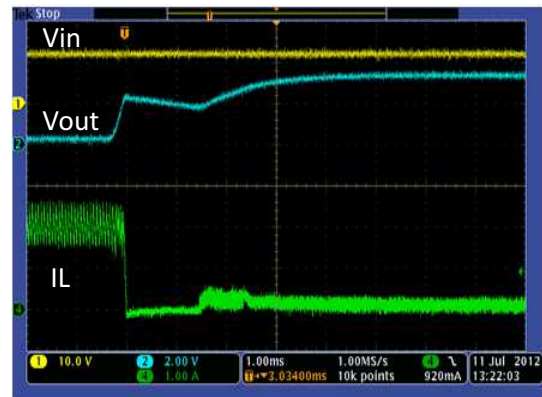


Figure 10. Short Circuit Recovery

OVERVIEW

The TPS5402 is a 28-V, 1.7-A, step-down (buck) converter with an integrated high-side N-channel MOSFET. To improve performance during line and load transients, the device implements a constant frequency, current mode control which reduces output capacitance and simplifies external frequency compensation design.

The TPS5402's switching frequency is adjustable with an external resistor or fixed by connecting the frequency program pin to GND or leaving it unconnected.

The TPS5402 starts switching at V_{IN} equal to 3.5 V. The operating current is 100 μ A typically when not switching and under no load. When the device is disabled, the supply current is 1 μ A typically.

The integrated 120-m Ω high-side MOSFET allows for high efficiency power supply designs with continuous output currents up to 1.7 A.

The TPS5402 reduces the external component count by integrating the boot recharge diode. The bias voltage for the integrated high-side MOSFET is supplied by an external capacitor on the BOOT to PH pins. The boot capacitor voltage is monitored by an UVLO circuit and will turn the high-side MOSFET off when the voltage falls below a preset threshold of 2.1 V typically.

By adding an external capacitor, the slow start time of the TPS5402 can be adjustable which enables flexible output filter selection. To improve the efficiency at light load conditions, the TPS5402 enters a special pulse skipping mode when the peak inductor current drops below 300 mA typically. The frequency foldback reduces the switching frequency during startup and over current conditions to help control the inductor current. The thermal shut down gives the additional protection under fault conditions.

DETAILED DESCRIPTION

Adjustable Frequency PWM Control

The TPS5402 uses an external resistor to adjust the switching frequency. Connecting the ROSC pin to ground fixes the switching frequency at 70 kHz, leaving it open gives 120-kHz switching frequency.

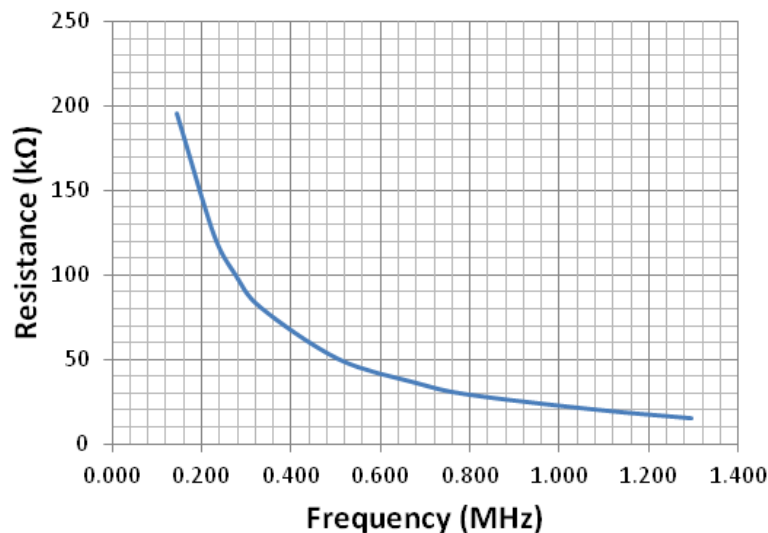


Figure 11. ROSC vs Switching Frequency

$$R_{OSC}(k\Omega) = 21.82 \cdot f_{SW}^{-1.167} \quad (1)$$

For operation at 300 kHz, an 85.5-k Ω resistor is required.

Pulse Skipping Mode

The TPS5402 is designed to operate in pulse skipping mode at light load currents to boost light load efficiency. When the peak inductor current is lower than 300 mA typically, the COMP pin voltage falls to 0.5 V typically and the device enters pulse skipping mode. When the device is in pulse skipping mode, the COMP pin voltage is clamped at 0.5 V internally which prevents the high side integrated MOSFET from switching. The peak inductor current must rise above 300 mA for the COMP pin voltage to rise above 0.5 V and exit pulse skipping mode. Since the integrated current comparator catches the peak inductor current only, the average load current entering pulse skipping mode varies with the applications and external output filters.

Voltage Reference (V_{SENSE})

The voltage reference system produces a $\pm 3\%$ accuracy voltage reference by scaling the output of a temperature stable bandgap circuit. The typical voltage reference is designed at 0.8 V.

Bootstrap Voltage (BOOT)

The TPS5402 has an integrated boot regulator and requires a 0.1- μ F ceramic capacitor between the BOOT and LX pins to provide the gate drive voltage for the high-side MOSFET. A ceramic capacitor with an X7R or X5R grade dielectric is recommended because of the stable characteristics over temperature and voltage. To improve drop out, the TPS5402 is designed to operate at 100% duty cycle as long as the BOOT to LX pin voltage is greater than 2.1 V typically.

Programmable Slow Start Using SS Pin

It is recommended to program the slow start time externally because no slow start time is implemented internally. The TPS5402 effectively uses the lower voltage of the internal voltage reference or the SS pin voltage as the power supply's reference voltage fed into the error amplifier and will regulate the output accordingly. A capacitor (C_{SS}) on the SS pin to ground implements a slow start time. The TPS5402 has an internal pull-up current source of 2 μ A that charges the external slow start capacitor. The equation for the slow start time (10% to 90%) is shown in [Equation 2](#). The internal V_{ref} is 0.8 V and the I_{SS} current is 2 μ A.

$$t_{ss}(ms) = \frac{C_{ss}(nF) \times V_{ref}(V)}{I_{ss}(\mu A)} \quad (2)$$

The slow start time should be set between 1 ms to 10 ms to ensure good start-up behavior. The slow start capacitor should be no more than 27 nF.

If during normal operation, the input voltage drops below the VIN UVLO threshold, or a thermal shutdown event occurs, the TPS5402 stops switching.

Error Amplifier

The TPS5402 has a transconductance amplifier for the error amplifier. The error amplifier compares the VSENSE voltage to the internal effective voltage reference presented at the input of the error amplifier. The transconductance of the error amplifier is 92 μ A/V during normal operation. Frequency compensation components are connected between the COMP pin and ground.

Slope Compensation

To prevent the sub-harmonic oscillations when operating the device at duty cycles greater than 50%, the TPS5402 adds a built-in slope compensation which is a compensating ramp to the switch current signal.

Overcurrent Protection and Frequency Shift

The TPS5402 implements current mode control that uses the COMP pin voltage to turn off the high-side MOSFET on a cycle by cycle basis. Every cycle the switch current and the COMP pin voltage are compared; when the peak inductor current intersects the COMP pin voltage, the high-side switch is turned off. During overcurrent conditions that pull the output voltage low, the error amplifier responds by driving the COMP pin high, causing the switch current to increase. The COMP pin has a maximum clamp internally, which limits the output current.

The TPS5402 provides robust protection during short circuits. There is potential for overcurrent runaway in the output inductor during a short circuit at the output. The TPS5402 solves this issue by increasing the off time during short circuit conditions by lowering the switching frequency. The switching frequency is divided by 8, 4, 2, and 1 as the voltage ramps from 0 V to 0.8 V on the VSENSE pin. The relationship between the switching frequency and the VSENSE pin voltage is shown in [Table 1](#).

Table 1. Switching Frequency Conditions

SWITCHING FREQUENCY	VSENSE PIN VOLTAGE
f_{SW}	$V_{SENSE} \geq 0.6 \text{ V}$
$f_{SW}/2$	$0.6 \text{ V} > V_{SENSE} \geq 0.4 \text{ V}$
$f_{SW}/4$	$0.4 \text{ V} > V_{SENSE} \geq 0.2 \text{ V}$
$f_{SW}/8$	$0.2 \text{ V} > V_{SENSE}$

Spread Spectrum

In order to reduce EMI, TPS5402 introduces frequency spread spectrum. The jittering span is $\pm 6\%$ of the switching frequency with 1/512 swing frequency.

Overvoltage Transient Protection

The TPS5402 incorporates an overvoltage transient protection (OVTP) circuit to minimize output voltage overshoot when recovering from output fault conditions or strong unload transients. The OVTP circuit includes an overvoltage comparator to compare the VSENSE pin voltage and internal thresholds. When the VSENSE pin voltage goes above $109\% \times V_{ref}$, the high-side MOSFET will be forced off. When the VSENSE pin voltage falls below $107\% \times V_{ref}$, the high-side MOSFET will be enabled again.

Inductor Selection

The higher operating frequency allows the use of smaller inductor and capacitor values. A higher frequency generally results in lower efficiency because of switching loss and MOSFET gate charge losses. In addition to this basic trade-off, the effect of the inductor value on ripple current and low current operation must also be considered. The ripple current depends on the inductor value. The inductor ripple current (i_L) decreases with higher inductance or higher frequency and increases with higher input voltage (V_{IN}). Accepting larger values of i_L allows the use of low inductances, but results in higher output voltage ripple and greater core losses.

To calculate the value of the output inductor, use [Equation 3](#). LIR is a coefficient that represents inductor peak-to-peak ripple to DC load current. It is recommended to set LIR to 0.1 ~ 0.3 for most applications.

Actual core loss of the inductor is independent of core size for a fixed inductor value, but it is very dependent on the inductance value selected. As inductance increases, core losses go down. Unfortunately, increased inductance requires more turns of wire and therefore copper losses will increase. Ferrite designs have very low core loss and are preferred for high switching frequencies, so design goals can concentrate on copper loss and preventing saturation. Ferrite core material saturates hard, which means that inductance collapses abruptly when the peak design current is exceeded. It results in an abrupt increase in inductor ripple current and consequent output voltage ripple. Do not allow the core to saturate. It is important that the RMS current and saturation current ratings are not exceeding the inductor specification. The RMS and peak inductor current can be calculated from [Equation 5](#) and [Equation 6](#).

$$L = \frac{V_{IN} - V_{OUT}}{I_O \cdot LIR} \cdot \frac{V_{OUT}}{V_{IN} \cdot f_{SW}} \quad (3)$$

$$\Delta i_L = \frac{V_{IN} - V_{OUT}}{I_O} \cdot \frac{V_{OUT}}{V_{IN} \cdot f_{SW}} \quad (4)$$

$$i_{LRMS} = \sqrt{I_O^2 + \frac{\left(\frac{V_{OUT} \cdot (V_{INmax} - V_{OUT})}{V_{INmax} \cdot L \cdot f_{SW}} \right)^2}{12}} \quad (5)$$

$$I_{Lpeak} = I_O + \frac{\Delta i_L}{2} \quad (6)$$

For this design example, use $LIR = 0.3$ and the inductor is calculated to be $5.40 \mu H$ with $V_{IN} = 12 V$. Choose $4.7 \mu H$ value for the standard inductor and the peak to peak inductor ripple is about 34% of 1-A DC load current.

Output Capacitor Selection

There are two primary considerations for selecting the value of the output capacitor. The output capacitors are selected to meet load transient and output ripple's requirements.

[Equation 7](#) gives the minimum output capacitance to meet the transient specification. For this example, $L = 4.7 \mu H$, $\Delta I_{OUT} = 1 A - 0.0 A = 1 A$ and $\Delta V_{OUT} = 500 mV$ (10% of regulated 5 V). Using these numbers gives a minimum capacitance of $1 \mu F$. A standard 22- μF ceramic is chosen in the design.

$$C_O > \frac{\Delta I_{OUT}^2 \cdot L}{2 \cdot V_{OUT} \cdot \Delta V_{OUT}} \quad (7)$$

The selection of C_O is driven by the effective series resistance (ESR). [Equation 8](#) calculates the minimum output capacitance needed to meet the output voltage ripple specification. Where f_{SW} is the switching frequency, ΔV_{OUT} is the maximum allowable output voltage ripple, and Δi_L is the inductor ripple current. In this case, the maximum output voltage ripple is 50 mV (1% of regulated 5 V). From [Equation 4](#), the output current ripple is 1 A. From [Equation 8](#), the minimum output capacitance meeting the output voltage ripple requirement is 2.5 μF with 3-m Ω ESR resistance.

$$C_O > \frac{1}{8 \cdot f_{SW}} \cdot \frac{1}{\frac{\Delta V_{OUT}}{\Delta i_L} - ESR} \quad (8)$$

After considering both requirements, for this example, one 22- μF , 6.3-V X7R ceramic capacitor with 3-m Ω ESR should be used.

Input Capacitor Selection

A minimum 10- μF X7R/X5R ceramic input capacitor is recommended to be added between V_{IN} and GND. These capacitors should be connected as close as physically possible to the input pins of the converters as they handle the RMS ripple current shown in [Equation 9](#). For this example, $I_{OUT} = 1 A$, $V_{OUT} = 5 V$, minimum $V_{INmin} = 9.6 V$, from [Equation 9](#), the input capacitors must support a ripple current of 1-A RMS.

$$I_{INRMS} = I_{OUT} \cdot \sqrt{\frac{V_{OUT}}{V_{INmin}} \cdot \frac{(V_{INmin} - V_{OUT})}{V_{INmin}}} \quad (9)$$

The input capacitance value determines the input ripple voltage of the regulator. The input voltage ripple can be calculated using [Equation 10](#). Using the design example values, $I_{OUTmax} = 1 A$, $C_{IN} = 10 \mu F$, $f_{SW} = 300 kHz$, yields an input voltage ripple of 83 mV.

$$\Delta V_{IN} = \frac{I_{OUTmax} \cdot 0.25}{C_{IN} \cdot f_{SW}} \quad (10)$$

To prevent large voltage transients, a low ESR capacitor sized for the maximum RMS current must be used.

Thermal Shutdown

The device implements an internal thermal shutdown to protect itself if the junction temperature exceeds 165°C. The thermal shutdown forces the device to stop switching when the junction temperature exceeds the thermal trip threshold. Once the die temperature decreases below 165°C, the device reinitiates the power up sequence.

PACKAGING INFORMATION

Orderable part number	Status (1)	Material type (2)	Package Pins	Package qty Carrier	RoHS (3)	Lead finish/ Ball material (4)	MSL rating/ Peak reflow (5)	Op temp (°C)	Part marking (6)
TPS5402DR	Active	Production	SOIC (D) 8	2500 LARGE T&R	Yes	NIPDAU	Level-1-260C-UNLIM	-40 to 125	T5402
TPS5402DR.A	Active	Production	SOIC (D) 8	2500 LARGE T&R	Yes	NIPDAU	Level-1-260C-UNLIM	-40 to 125	T5402

⁽¹⁾ **Status:** For more details on status, see our [product life cycle](#).

⁽²⁾ **Material type:** When designated, preproduction parts are prototypes/experimental devices, and are not yet approved or released for full production. Testing and final process, including without limitation quality assurance, reliability performance testing, and/or process qualification, may not yet be complete, and this item is subject to further changes or possible discontinuation. If available for ordering, purchases will be subject to an additional waiver at checkout, and are intended for early internal evaluation purposes only. These items are sold without warranties of any kind.

⁽³⁾ **RoHS values:** Yes, No, RoHS Exempt. See the [TI RoHS Statement](#) for additional information and value definition.

⁽⁴⁾ **Lead finish/Ball material:** Parts may have multiple material finish options. Finish options are separated by a vertical ruled line. Lead finish/Ball material values may wrap to two lines if the finish value exceeds the maximum column width.

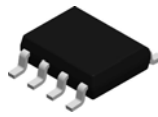
⁽⁵⁾ **MSL rating/Peak reflow:** The moisture sensitivity level ratings and peak solder (reflow) temperatures. In the event that a part has multiple moisture sensitivity ratings, only the lowest level per JEDEC standards is shown. Refer to the shipping label for the actual reflow temperature that will be used to mount the part to the printed circuit board.

⁽⁶⁾ **Part marking:** There may be an additional marking, which relates to the logo, the lot trace code information, or the environmental category of the part.

Multiple part markings will be inside parentheses. Only one part marking contained in parentheses and separated by a "~" will appear on a part. If a line is indented then it is a continuation of the previous line and the two combined represent the entire part marking for that device.

Important Information and Disclaimer:The information provided on this page represents TI's knowledge and belief as of the date that it is provided. TI bases its knowledge and belief on information provided by third parties, and makes no representation or warranty as to the accuracy of such information. Efforts are underway to better integrate information from third parties. TI has taken and continues to take reasonable steps to provide representative and accurate information but may not have conducted destructive testing or chemical analysis on incoming materials and chemicals. TI and TI suppliers consider certain information to be proprietary, and thus CAS numbers and other limited information may not be available for release.

In no event shall TI's liability arising out of such information exceed the total purchase price of the TI part(s) at issue in this document sold by TI to Customer on an annual basis.

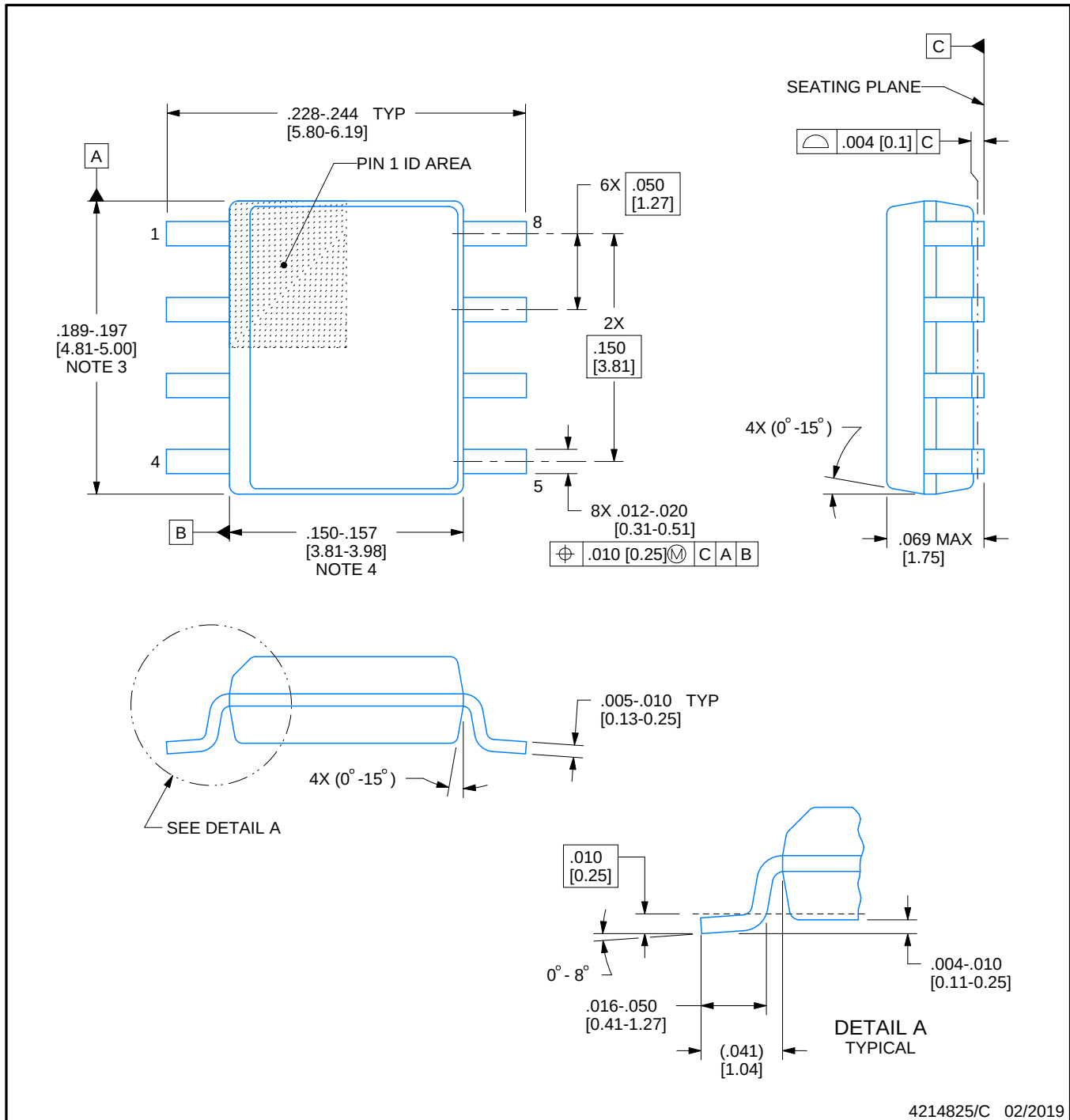


D0008A

PACKAGE OUTLINE

SOIC - 1.75 mm max height

SMALL OUTLINE INTEGRATED CIRCUIT



4214825/C 02/2019

NOTES:

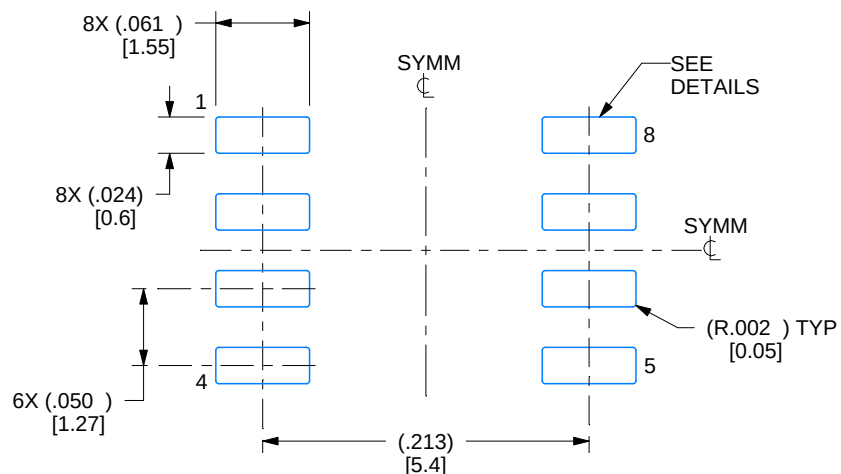
1. Linear dimensions are in inches [millimeters]. Dimensions in parenthesis are for reference only. Controlling dimensions are in inches. Dimensioning and tolerancing per ASME Y14.5M.
2. This drawing is subject to change without notice.
3. This dimension does not include mold flash, protrusions, or gate burrs. Mold flash, protrusions, or gate burrs shall not exceed .006 [0.15] per side.
4. This dimension does not include interlead flash.
5. Reference JEDEC registration MS-012, variation AA.

EXAMPLE BOARD LAYOUT

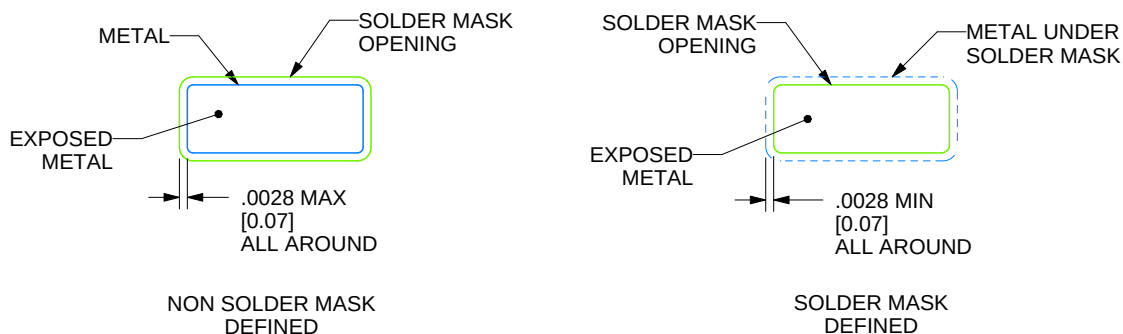
D0008A

SOIC - 1.75 mm max height

SMALL OUTLINE INTEGRATED CIRCUIT



LAND PATTERN EXAMPLE
EXPOSED METAL SHOWN
SCALE:8X



SOLDER MASK DETAILS

4214825/C 02/2019

NOTES: (continued)

6. Publication IPC-7351 may have alternate designs.

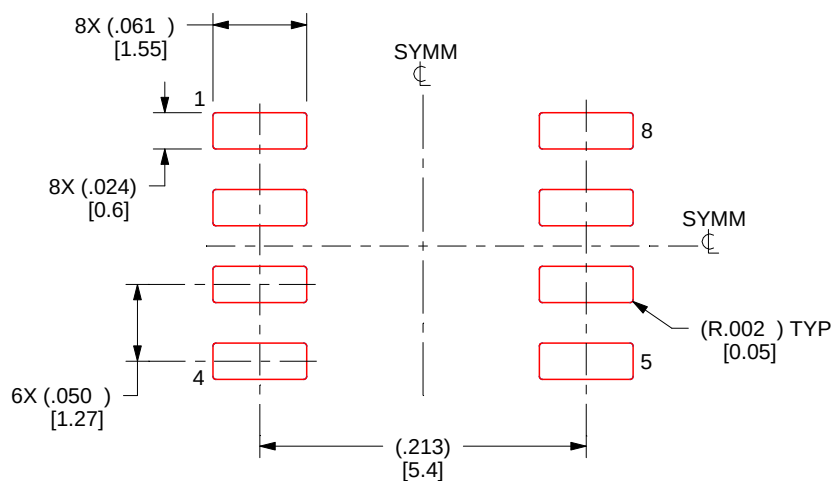
7. Solder mask tolerances between and around signal pads can vary based on board fabrication site.

EXAMPLE STENCIL DESIGN

D0008A

SOIC - 1.75 mm max height

SMALL OUTLINE INTEGRATED CIRCUIT



SOLDER PASTE EXAMPLE
BASED ON .005 INCH [0.125 MM] THICK STENCIL
SCALE:8X

4214825/C 02/2019

NOTES: (continued)

8. Laser cutting apertures with trapezoidal walls and rounded corners may offer better paste release. IPC-7525 may have alternate design recommendations.
9. Board assembly site may have different recommendations for stencil design.

重要通知和免责声明

TI“按原样”提供技术和可靠性数据（包括数据表）、设计资源（包括参考设计）、应用或其他设计建议、网络工具、安全信息和其他资源，不保证没有瑕疵且不做任何明示或暗示的担保，包括但不限于对适销性、与某特定用途的适用性或不侵犯任何第三方知识产权的暗示担保。

这些资源可供使用 TI 产品进行设计的熟练开发人员使用。您将自行承担以下全部责任：(1) 针对您的应用选择合适的 TI 产品，(2) 设计、验证并测试您的应用，(3) 确保您的应用满足相应标准以及任何其他安全、安保法规或其他要求。

这些资源如有变更，恕不另行通知。TI 授权您仅可将这些资源用于研发本资源所述的 TI 产品的相关应用。严禁以其他方式对这些资源进行复制或展示。您无权使用任何其他 TI 知识产权或任何第三方知识产权。对于因您对这些资源的使用而对 TI 及其代表造成的任何索赔、损害、成本、损失和债务，您将全额赔偿，TI 对此概不负责。

TI 提供的产品受 [TI 销售条款](#)、[TI 通用质量指南](#) 或 [ti.com](#) 上其他适用条款或 TI 产品随附的其他适用条款的约束。TI 提供这些资源并不会扩展或以其他方式更改 TI 针对 TI 产品发布的适用的担保或担保免责声明。除非德州仪器 (TI) 明确将某产品指定为定制产品或客户特定产品，否则其产品均为按确定价格收入目录的标准通用器件。

TI 反对并拒绝您可能提出的任何其他或不同的条款。

版权所有 © 2025，德州仪器 (TI) 公司

最后更新日期：2025 年 10 月