

# INA819 35- $\mu\text{V}$ Offset, 8-nV/ $\sqrt{\text{Hz}}$ Noise, Low-Power, Precision Instrumentation Amplifier

## 1 Features

- Low offset voltage: 10  $\mu\text{V}$  (typ), 35  $\mu\text{V}$  (max)
- Gain drift: 5 ppm/ $^{\circ}\text{C}$  ( $G = 1$ ), 35 ppm/ $^{\circ}\text{C}$  ( $G > 1$ ) (max)
- Noise: 8 nV/ $\sqrt{\text{Hz}}$
- Bandwidth: 2 MHz ( $G = 1$ ), 270 kHz ( $G = 100$ )
- Stable with 1-nF capacitive loads
- Inputs protected up to  $\pm 60\text{ V}$
- Common-mode rejection: 110 dB,  $G = 10$  (min)
- Power supply rejection: 110 dB,  $G = 1$  (min)
- Supply current: 385  $\mu\text{A}$  (max)
- Supply range:
  - Single supply: 4.5 V to 36 V
  - Dual supply:  $\pm 2.25\text{ V}$  to  $\pm 18\text{ V}$
- Specified temperature range:  $-40^{\circ}\text{C}$  to  $+125^{\circ}\text{C}$
- Packages: 8-pin SOIC, VSSOP, WSON

## 2 Applications

- [Analog input module](#)
- [Flow transmitter](#)
- [Battery test](#)
- [LCD test](#)
- [Electrocardiogram \(ECG\)](#)
- [Surgical equipment](#)
- [Process analytics \(pH, gas, concentration, force and humidity\)](#)

## 3 Description

The INA819 is a high-precision instrumentation amplifier that offers low power consumption and operates over a very wide single-supply or dual-supply range. A single external resistor sets any gain from 1 to 10,000. The device offers high precision as a result of super-beta input transistors, which provide exceptionally low input offset voltage, offset voltage drift, input bias current, input voltage, and current noise. Additional circuitry protects the inputs against overvoltage up to  $\pm 60\text{ V}$ .

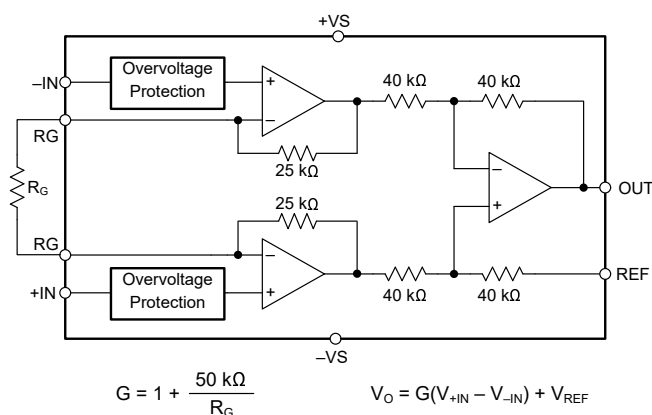
The INA819 is optimized to provide a high common-mode rejection ratio. At  $G = 1$ , the common-mode rejection ratio exceeds 90 dB across the full input common-mode range. The device is designed for low-voltage operation from a 4.5-V single supply, as well as dual supplies up to  $\pm 18\text{ V}$ .

The INA819 is available in 8-pin SOIC, VSSOP, and WSON packages, and is specified over the  $-40^{\circ}\text{C}$  to  $+125^{\circ}\text{C}$  temperature range.

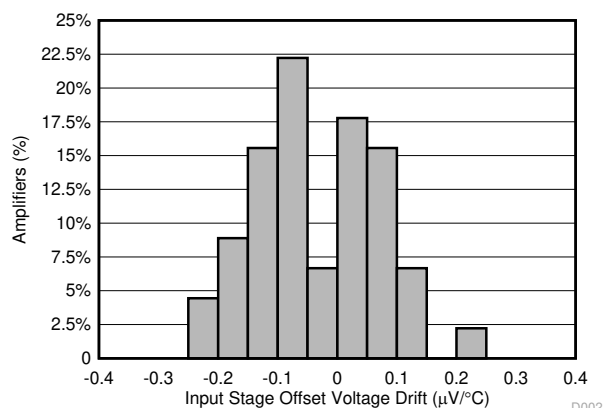
### Device Information<sup>(1)</sup>

PART NUMBER	PACKAGE	BODY SIZE (NOM)
INA819	SOIC (8)	4.90 mm $\times$ 3.91 mm
	VSSOP (8)	3.00 mm $\times$ 3.00 mm
	WSON (8)	3.00 mm $\times$ 3.00 mm

(1) For all available packages, see the package option addendum at the end of the data sheet.



INA819 Simplified Internal Schematic



Typical Distribution of Input Stage Offset Voltage Drift

D002



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## 4 Revision History

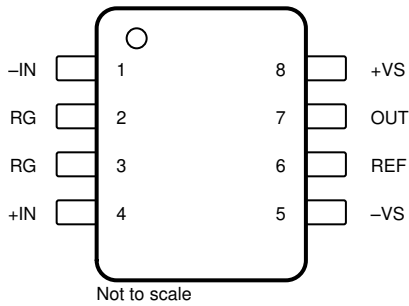
NOTE: Page numbers for previous revisions may differ from page numbers in the current version.

<b>Changes from Revision C (June 2020) to Revision D (April 2022)</b>	<b>Page</b>
• Changed input stage offset voltage specification for INA819DRG from 10 $\mu\text{V}$ typical to 6 $\mu\text{V}$ typical, and from 35 $\mu\text{V}$ maximum to 30 $\mu\text{V}$ maximum, in <i>Typical Characteristics</i> .....	6
• Changed maximum input stage offset voltage vs temperature specification for INA819DRG from 0.4 $\mu\text{V}/^\circ\text{C}$ to 0.35 $\mu\text{V}/^\circ\text{C}$ in <i>Typical Characteristics</i> .....	6
• Changed Figures 7-10 and 7-11 to correct units from nA to pA.....	8
• Changed input common-mode range calculator link from outdated Common-Mode Input Range Calculator for Instrumentation Amplifiers to Analog Engineers Calculator.....	22
<b>Changes from Revision B (July 2019) to Revision C (June 2020)</b>	<b>Page</b>
• Added DRG (WSON) package and associated content to data sheet.....	1
• Added row for thermal pad to <i>Pin Functions</i> table .....	4
• Added bullet regarding exposed thermal pad to end of <i>Layout Guidelines</i> section .....	32
<b>Changes from Revision A (May 2019) to Revision B (July 2019)</b>	<b>Page</b>
• Changed DGK (VSSOP) package from advanced information (preview) to production data (active).....	1
<b>Changes from Revision * (December 2018) to Revision A (April 2019)</b>	<b>Page</b>
• Added 8-pin DGK (VSSOP) advanced information package and associated content to data sheet.....	1
• Changed <i>Applications</i> bullets .....	1

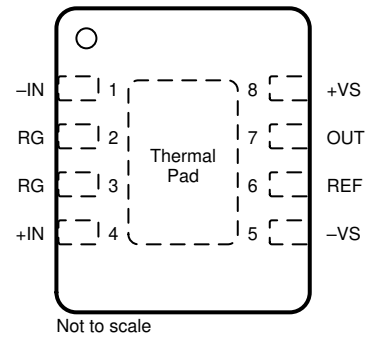
## 5 Device Comparison Table

DEVICE	DESCRIPTION	GAIN EQUATION	RG PINS AT PIN
<a href="#">INA819</a>	35- $\mu$ V Offset, 0.4- $\mu$ V/ $^{\circ}$ C $V_{OS}$ Drift, 8-nV/ $\sqrt{\text{Hz}}$ Noise, Low-Power, Precision Instrumentation Amplifier	$G = 1 + 50 \text{ k}\Omega / R_G$	2, 3
<a href="#">INA818</a>	35- $\mu$ V Offset, 0.4- $\mu$ V/ $^{\circ}$ C $V_{OS}$ Drift, 8-nV/ $\sqrt{\text{Hz}}$ Noise, Low-Power, Precision Instrumentation Amplifier	$G = 1 + 50 \text{ k}\Omega / R_G$	1, 8
<a href="#">INA821</a>	35- $\mu$ V Offset, 0.4- $\mu$ V/ $^{\circ}$ C $V_{OS}$ Drift, 7-nV/ $\sqrt{\text{Hz}}$ Noise, High-Bandwidth, Precision Instrumentation Amplifier	$G = 1 + 49.4 \text{ k}\Omega / R_G$	2, 3
<a href="#">INA828</a>	50- $\mu$ V Offset, 0.5- $\mu$ V/ $^{\circ}$ C $V_{OS}$ Drift, 7-nV/ $\sqrt{\text{Hz}}$ Noise, Low-Power, Precision Instrumentation Amplifier	$G = 1 + 50 \text{ k}\Omega / R_G$	1, 8
<a href="#">INA333</a>	25- $\mu$ V $V_{OS}$ , 0.1- $\mu$ V/ $^{\circ}$ C $V_{OS}$ Drift, 1.8-V to 5-V, RRO, 50- $\mu$ A $I_Q$ , Chopper-Stabilized INA	$G = 1 + 100 \text{ k}\Omega / R_G$	1, 8
<a href="#">PGA280</a>	20-mV to $\pm 10$ -V Programmable Gain IA With 3-V or 5-V Differential Output; Analog Supply up to $\pm 18$ V	Digital programmable	N/A
<a href="#">INA159</a>	$G = 0.2$ V Differential Amplifier for $\pm 10$ -V to 3-V and 5-V Conversion	$G = 0.2 \text{ V/V}$	N/A
<a href="#">PGA112</a>	Precision Programmable Gain Op Amp With SPI	Digital programmable	N/A

## 6 Pin Configuration and Functions



**Figure 6-1. D (8-Pin SOIC) and DGK (8-Pin VSSOP) Packages, Top View**



**Figure 6-2. DRG Package, 8-Pin WSON, Top View**

**Table 6-1. Pin Functions**

PIN		TYPE	DESCRIPTION
NAME	NO.		
-IN	1	Input	Negative (inverting) input
+IN	4	Input	Positive (noninverting) input
OUT	7	Output	Output
RG	2, 3	—	Gain setting pin. Place a gain resistor between pin 2 and pin 3.
REF	6	Input	Reference input. This pin must be driven by a low impedance source.
-VS	5	—	Negative supply
+VS	8	—	Positive supply
Thermal pad	—	—	Thermal pad internally connected to -VS. Connect externally to -VS or leave floating.

## 7 Specifications

### 7.1 Absolute Maximum Ratings

over operating free-air temperature range (unless otherwise noted)<sup>(1)</sup>

	MIN	MAX	UNIT
Supply voltage dual supply, $V_S = (V+) - (V-)$		±20	V
Supply voltage single supply, $V_S = (V+) - (V-)$		40	V
Signal input pins	-60	60	V
VREF pin	-20	20	V
Signal output pins maximum voltage	$(-V_S) - 0.5$	$(+V_S) + 0.5$	V
Signal output pins maximum current	-50	50	mA
Output short-circuit <sup>(2)</sup>	Continuous		
Operating Temperature, $T_A$	-50	150	°C
Junction Temperature, $T_J$		175	°C
Storage Temperature, $T_{stg}$	-65	150	°C

- (1) Stresses beyond those listed under *Absolute Maximum Ratings* may cause permanent damage to the device. These are stress ratings only, which do not imply functional operation of the device at these or any other conditions beyond those indicated under *Recommended Operating Conditions*. Exposure to absolute-maximum-rated conditions for extended periods may affect device reliability.
- (2) Short-circuit to  $V_S / 2$ .

### 7.2 ESD Ratings

			VALUE	UNIT
$V_{(ESD)}$	Electrostatic discharge	Human-body model (HBM), per ANSI/ESDA/JEDEC JS-001 <sup>(1)</sup>	±1500	V
		Charged-device model (CDM), per JEDEC specification JESD22-C101 <sup>(2)</sup>	±750	

- (1) JEDEC document JEP155 states that 500-V HBM allows safe manufacturing with a standard ESD control process.
- (2) JEDEC document JEP157 states that 250-V CDM allows safe manufacturing with a standard ESD control process.

### 7.3 Recommended Operating Conditions

over operating free-air temperature range (unless otherwise noted)

		MIN	MAX	UNIT
Supply voltage, $V_S$	Single-supply	4.5	36	V
	Dual-supply	±2.25	±18	
Specified temperature, $T_A$	Specified temperature	-40	125	°C

### 7.4 Thermal Information

THERMAL METRIC <sup>(1)</sup>		INA819			UNIT
		D (SOIC)	DGK (VSSOP)	DRG (WSON)	
		8 PINS	8 PINS	8 PINS	
$R_{\theta JA}$	Junction-to-ambient thermal resistance	119.6	215.4	55.6	°C/W
$R_{\theta JC(top)}$	Junction-to-case (top) thermal resistance	66.3	66.3	57.9	°C/W
$R_{\theta JB}$	Junction-to-board thermal resistance	61.9	97.8	28.6	°C/W
$\psi_{JT}$	Junction-to-top characterization parameter	20.5	10.5	1.8	°C/W
$\psi_{JB}$	Junction-to-board characterization parameter	61.4	96.1	28.6	°C/W
$R_{\theta JC(bot)}$	Junction-to-case (bottom) thermal resistance	N/A	N/A	12.1	°C/W

- (1) For more information about traditional and new thermal metrics, see the [Semiconductor and IC Package Thermal Metrics](#) application report.

### 7.5 Electrical Characteristics

at  $T_A = 25^\circ\text{C}$ ,  $V_S = \pm 15\text{ V}$ ,  $R_L = 10\text{ k}\Omega$ ,  $V_{REF} = 0\text{ V}$ , and  $G = 1$  (unless otherwise noted)

PARAMETER		TEST CONDITIONS		MIN	TYP	MAX	UNIT	
<b>INPUT</b>								
$V_{OSI}$	Input stage offset voltage <sup>(1) (3)</sup>		INA819ID		10	35	$\mu\text{V}$	
			INA819IDGK			40		
			INA819IDRG		6	30		
		$T_A = -40^\circ\text{C to } +125^\circ\text{C}^{(2)}$	INA819ID, INA819DRG				75	$\mu\text{V}/^\circ\text{C}$
			INA819IDGK				80	
			vs temperature, $T_A = -40^\circ\text{C to } +125^\circ\text{C}$	INA819D, INA819DGK				
INA819DRG					0.35			
$V_{OSO}$	Output stage offset voltage <sup>(1) (3)</sup>				50	300	$\mu\text{V}$	
					$T_A = -40^\circ\text{C to } +125^\circ\text{C}^{(2)}$			
		vs temperature, $T_A = -40^\circ\text{C to } +125^\circ\text{C}$					5	$\mu\text{V}/^\circ\text{C}$
PSRR	Power-supply rejection ratio		$G = 1, \text{ RTI}$	110	120	dB		
			$G = 10, \text{ RTI}$	114	130			
			$G = 100, \text{ RTI}$	130	135			
			$G = 1000, \text{ RTI}$	136	140			
$Z_{id}$	Differential impedance				100    1	$\text{G}\Omega \parallel \text{pF}$		
$Z_{ic}$	Common-mode impedance				100    4	$\text{G}\Omega \parallel \text{pF}$		
	RFI filter, -3-dB frequency				32	MHz		
$V_{CM}$	Operating input range <sup>(4)</sup>			$(V-) + 2$		$(V+) - 2$	V	
		$V_S = \pm 2.25\text{ V to } \pm 18\text{ V}, T_A = -40^\circ\text{C to } +125^\circ\text{C}$			See <a href="#">Figure 7-51</a> through <a href="#">Figure 7-54</a>			
	Input overvoltage range					$\pm 60$	V	
CMRR	Common-mode rejection ratio		At DC to 60 Hz, RTI, $V_{CM} = (V-) + 2\text{ V to } (V+) - 2\text{ V}, G = 1$	90	105	dB		
			At DC to 60 Hz, RTI, $V_{CM} = (V-) + 2\text{ V to } (V+) - 2\text{ V}, G = 10$	110	125			
			At DC to 60 Hz, RTI, $V_{CM} = (V-) + 2\text{ V to } (V+) - 2\text{ V}, G = 100$	130	145			
			At DC to 60 Hz, RTI, $V_{CM} = (V-) + 2\text{ V to } (V+) - 2\text{ V}, G = 1000$	140	150			
<b>BIAS CURRENT</b>								
$I_B$	Input bias current	$V_{CM} = V_S / 2$			0.15	0.5	nA	
		$T_A = -40^\circ\text{C to } +125^\circ\text{C}$				2		
$I_{OS}$	Input offset current	$V_{CM} = V_S / 2$			0.15	0.5	nA	
		$T_A = -40^\circ\text{C to } +125^\circ\text{C}$				2		
<b>NOISE VOLTAGE</b>								
$e_{NI}$	Input stage voltage noise <sup>(6)</sup>	$f = 1\text{ kHz}, G = 100, R_S = 0\ \Omega$			8		$\text{nV}/\sqrt{\text{Hz}}$	
		$f_B = 0.1\text{ Hz to } 10\text{ Hz}, G = 100, R_S = 0\ \Omega$			0.19		$\mu\text{V}_{PP}$	
$e_{NO}$	Output stage voltage noise <sup>(6)</sup>	$f = 1\text{ kHz}, R_S = 0\ \Omega$			80		$\text{nV}/\sqrt{\text{Hz}}$	
		$f_B = 0.1\text{ Hz to } 10\text{ Hz}, R_S = 0\ \Omega$			2.6		$\mu\text{V}_{PP}$	
$I_n$	Noise current	$f = 1\text{ kHz}$			130		$\text{fA}/\sqrt{\text{Hz}}$	
		$f_B = 0.1\text{ Hz to } 10\text{ Hz}, G = 100$			4.7		$\text{pA}_{PP}$	

## 7.5 Electrical Characteristics (continued)

at  $T_A = 25^\circ\text{C}$ ,  $V_S = \pm 15\text{ V}$ ,  $R_L = 10\text{ k}\Omega$ ,  $V_{REF} = 0\text{ V}$ , and  $G = 1$  (unless otherwise noted)

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
<b>GAIN</b>						
	Gain equation		1 + (50 k $\Omega$ / R <sub>G</sub> )			V/V
G	Gain		1		10000	V/V
GE	Gain error	G = 1, V <sub>O</sub> = $\pm 10\text{ V}$		$\pm 0.005\%$	$\pm 0.025\%$	
		G = 10, V <sub>O</sub> = $\pm 10\text{ V}$		$\pm 0.025\%$	$\pm 0.15\%$	
		G = 100, V <sub>O</sub> = $\pm 10\text{ V}$		$\pm 0.025\%$	$\pm 0.15\%$	
		G = 1000, V <sub>O</sub> = $\pm 10\text{ V}$		$\pm 0.05\%$		
	Gain vs temperature <sup>(5)</sup>	G = 1, T <sub>A</sub> = $-40^\circ\text{C}$ to $+125^\circ\text{C}$			$\pm 5$	ppm/ $^\circ\text{C}$
		G > 1, T <sub>A</sub> = $-40^\circ\text{C}$ to $+125^\circ\text{C}$			$\pm 35$	
	Gain nonlinearity	G = 1 to 10, V <sub>O</sub> = $-10\text{ V}$ to $+10\text{ V}$ , R <sub>L</sub> = 10 k $\Omega$		1	10	ppm
		G = 100, V <sub>O</sub> = $-10\text{ V}$ to $+10\text{ V}$ , R <sub>L</sub> = 10 k $\Omega$			15	
		G = 1000, V <sub>O</sub> = $-10\text{ V}$ to $+10\text{ V}$ , R <sub>L</sub> = 10 k $\Omega$		10		
		G = 1 to 100, V <sub>O</sub> = $-10\text{ V}$ to $+10\text{ V}$ , R <sub>L</sub> = 2 k $\Omega$		30		
<b>OUTPUT</b>						
	Voltage swing		(V-) + 0.15		(V+) - 0.15	V
	Load capacitance stability			1000		pF
Z <sub>O</sub>	Closed-loop output impedance	f = 10 kHz		5.0		$\Omega$
I <sub>SC</sub>	Short-circuit current	Continuous to V <sub>S</sub> / 2		$\pm 20$		mA
<b>FREQUENCY RESPONSE</b>						
BW	Bandwidth, -3 dB	G = 1		2.0		MHz
		G = 10		890		kHz
		G = 100		270		
		G = 1000		30		
SR	Slew rate	G = 1, V <sub>O</sub> = $\pm 10\text{ V}$		0.9		V/ $\mu\text{s}$
t <sub>S</sub>	Settling time	0.01%, G = 1 to 100, V <sub>STEP</sub> = 10 V		12		$\mu\text{s}$
		0.01%, G = 1000, V <sub>STEP</sub> = 10 V		40		
		0.001%, G = 1 to 100, V <sub>STEP</sub> = 10 V		16		
		0.001%, G = 1000, V <sub>STEP</sub> = 10 V		60		
<b>REFERENCE INPUT</b>						
R <sub>IN</sub>	Input impedance			40		k $\Omega$
	Voltage range		(V-)		(V+)	V
	Gain to output			1		V/V
	Reference gain error			0.01%		
<b>POWER SUPPLY</b>						
I <sub>Q</sub>	Quiescent current	V <sub>IN</sub> = 0 V		350	385	$\mu\text{A}$
		vs temperature, T <sub>A</sub> = $-40^\circ\text{C}$ to $+125^\circ\text{C}$			520	

- (1) Total offset, referred-to-input (RTI):  $V_{OS} = (V_{OSI}) + (V_{OSO} / G)$ .
- (2) Specified by characterization.
- (3) Offset drifts are uncorrelated. Input-referred offset drift is calculated using:  $\Delta V_{OS(RTI)} = \sqrt{[\Delta V_{OSI}]^2 + (\Delta V_{OSO} / G)^2}$ .
- (4) Input voltage range of the Instrumentation Amplifier input stage. The input range depends on the common-mode voltage, differential voltage, gain, and reference voltage.
- (5) The values specified for G > 1 do not include the effects of the external gain-setting resistor, R<sub>G</sub>.
- (6) Total RTI voltage noise is equal to:  $e_{N(RTI)} = \sqrt{[e_{NI}]^2 + (e_{NO} / G)^2}$ .

## 7.6 Typical Characteristics

at  $T_A = 25^\circ\text{C}$ ,  $V_S = \pm 15\text{ V}$ ,  $R_L = 10\text{ k}\Omega$ ,  $V_{REF} = 0\text{ V}$ , and  $G = 1$  (unless otherwise noted)

**Table 7-1. Table of Graphs**

DESCRIPTION	FIGURE
Typical Distribution of Input Stage Offset Voltage	<a href="#">Figure 7-1</a>
Typical Distribution of Input Stage Offset Voltage Drift	<a href="#">Figure 7-2</a>
Typical Distribution of Output Stage Offset Voltage	<a href="#">Figure 7-3</a>
Typical Distribution of Output Stage Offset Voltage Drift	<a href="#">Figure 7-4</a>
Input Stage Offset Voltage vs Temperature	<a href="#">Figure 7-5</a>
Output Stage Offset Voltage vs Temperature	<a href="#">Figure 7-6</a>
Typical Distribution of Input Bias Current, $T_A = 25^\circ\text{C}$	<a href="#">Figure 7-7</a>
Typical Distribution of Input Bias Current, $T_A = 90^\circ\text{C}$	<a href="#">Figure 7-8</a>
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Input Offset Current vs Temperature	<a href="#">Figure 7-11</a>
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Typical CMRR Distribution, $G = 10$	<a href="#">Figure 7-13</a>
CMRR vs Temperature, $G = 1$	<a href="#">Figure 7-14</a>
CMRR vs Temperature, $G = 10$	<a href="#">Figure 7-15</a>
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Negative PSRR vs Frequency (RTI)	<a href="#">Figure 7-20</a>
Gain vs Frequency	<a href="#">Figure 7-21</a>
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Current Noise Spectral Density vs Frequency (RTI)	<a href="#">Figure 7-23</a>
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Typical Distribution of Gain Error, $G = 10$	<a href="#">Figure 7-29</a>
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Gain Error vs Temperature, $G = 10$	<a href="#">Figure 7-31</a>
Supply Current vs Temperature	<a href="#">Figure 7-32</a>
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Gain Nonlinearity, $G = 10$	<a href="#">Figure 7-34</a>
Offset Voltage vs Negative Common-Mode Voltage	<a href="#">Figure 7-35</a>
Offset Voltage vs Positive Common-Mode Voltage	<a href="#">Figure 7-36</a>
Positive Output Voltage Swing vs Output Current	<a href="#">Figure 7-37</a>
Negative Output Voltage Swing vs Output Current	<a href="#">Figure 7-38</a>
Short Circuit Current vs Temperature	<a href="#">Figure 7-39</a>
Large-Signal Frequency Response	<a href="#">Figure 7-40</a>
THD+N vs Frequency	<a href="#">Figure 7-41</a>
Overshoot vs Capacitive Loads	<a href="#">Figure 7-42</a>
Small-Signal Response, $G = 1$	<a href="#">Figure 7-43</a>

## 7.6 Typical Characteristics

at  $T_A = 25^\circ\text{C}$ ,  $V_S = \pm 15\text{ V}$ ,  $R_L = 10\text{ k}\Omega$ ,  $V_{REF} = 0\text{ V}$ , and  $G = 1$  (unless otherwise noted)

**Table 7-1. Table of Graphs (continued)**

DESCRIPTION	FIGURE
Small-Signal Response, $G = 10$	<a href="#">Figure 7-44</a>
Small-Signal Response, $G = 100$	<a href="#">Figure 7-45</a>
Small-Signal Response, $G = 1000$	<a href="#">Figure 7-46</a>
Large Signal Step Response	<a href="#">Figure 7-47</a>
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Differential-Mode EMI Rejection Ratio	<a href="#">Figure 7-49</a>
Common-Mode EMI Rejection Ratio	<a href="#">Figure 7-50</a>
Input Common-Mode Voltage vs Output Voltage, $G = 1$ , $V_S = 5\text{ V}$	<a href="#">Figure 7-51</a>
Input Common-Mode Voltage vs Output Voltage, $G = 100$ , $V_S = 5\text{ V}$	<a href="#">Figure 7-52</a>
Input Common-Mode Voltage vs Output Voltage, $V_S = \pm 5\text{ V}$	<a href="#">Figure 7-53</a>
Input Common-Mode Voltage vs Output Voltage, $V_S = \pm 15\text{ V}$	<a href="#">Figure 7-54</a>

## 7.6 Typical Characteristics

at  $T_A = 25^\circ\text{C}$ ,  $V_S = \pm 15\text{ V}$ ,  $R_L = 10\text{ k}\Omega$ ,  $V_{REF} = 0\text{ V}$ , and  $G = 1$  (unless otherwise noted)

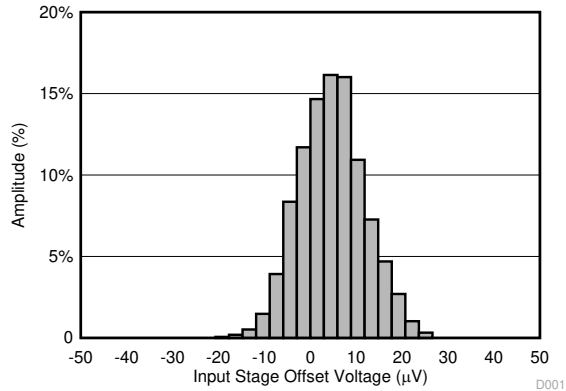


Figure 7-1. Typical Distribution of Input Stage Offset Voltage

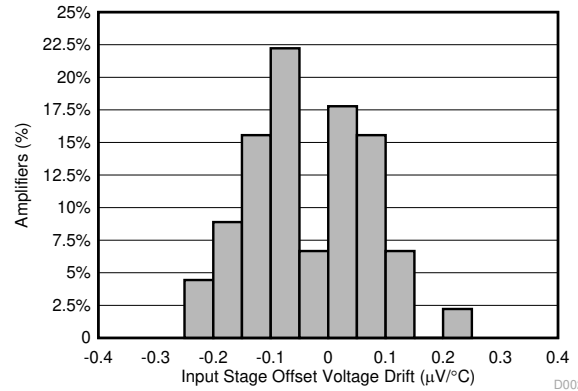


Figure 7-2. Typical Distribution of Input Stage Offset Voltage Drift

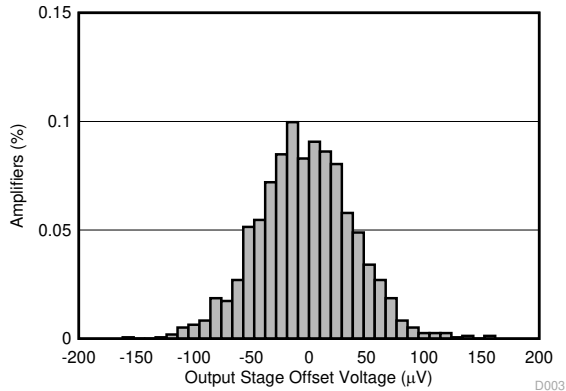


Figure 7-3. Typical Distribution of Output Stage Offset Voltage

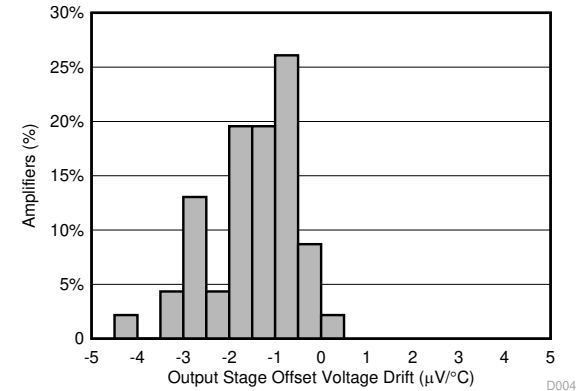


Figure 7-4. Typical Distribution of Output Stage Offset Voltage Drift

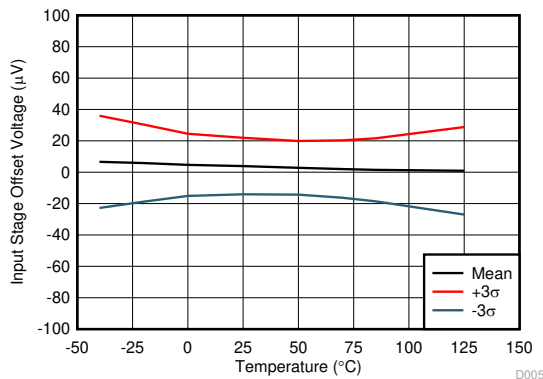


Figure 7-5. Input Stage Offset Voltage vs Temperature

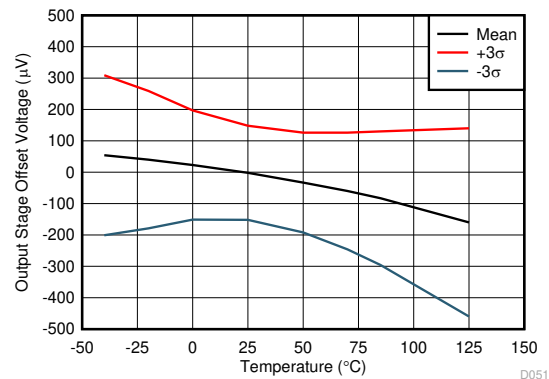
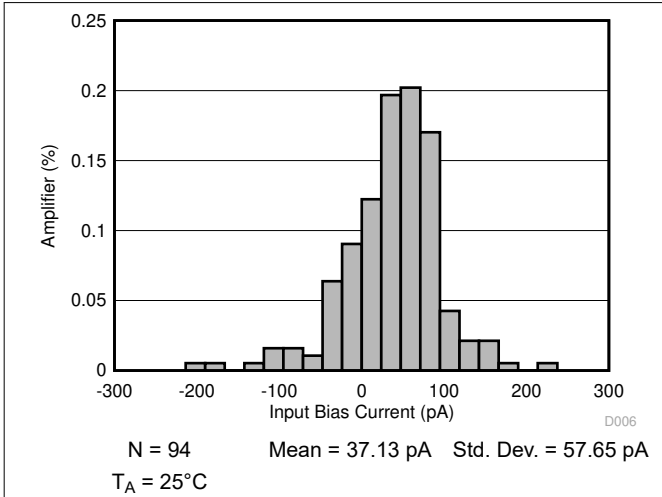


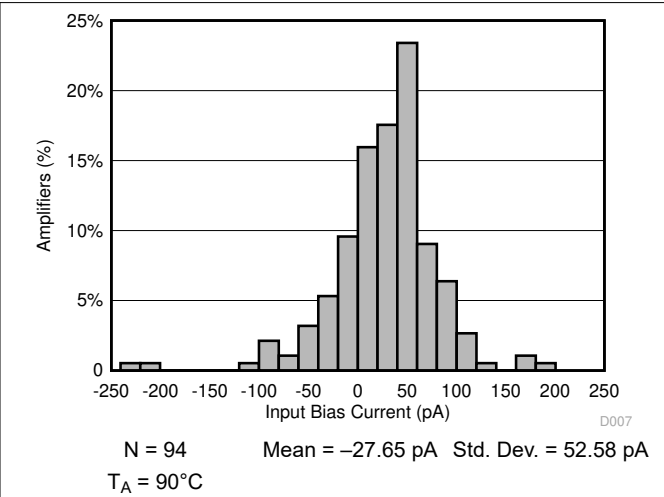
Figure 7-6. Output Stage Offset Voltage vs Temperature

### 7.6 Typical Characteristics (continued)

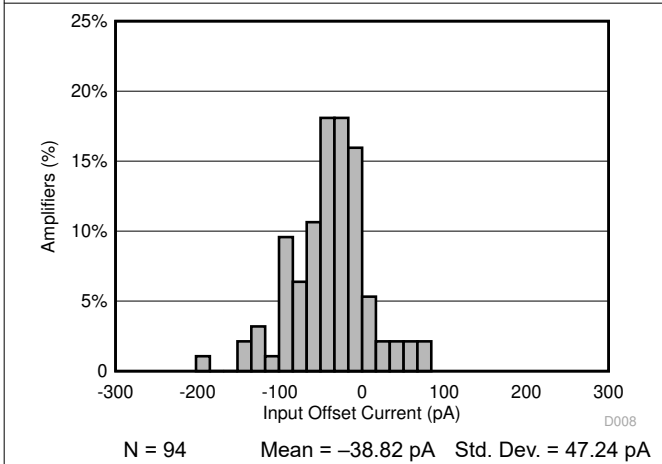
at  $T_A = 25^\circ\text{C}$ ,  $V_S = \pm 15\text{ V}$ ,  $R_L = 10\text{ k}\Omega$ ,  $V_{REF} = 0\text{ V}$ , and  $G = 1$  (unless otherwise noted)



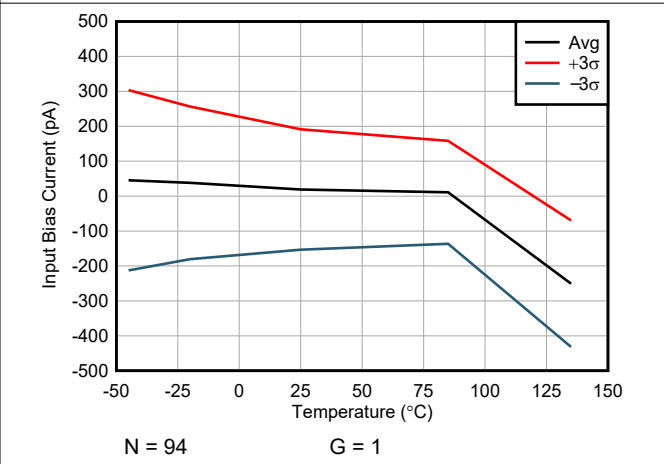
**Figure 7-7. Typical Distribution of Input Bias Current**



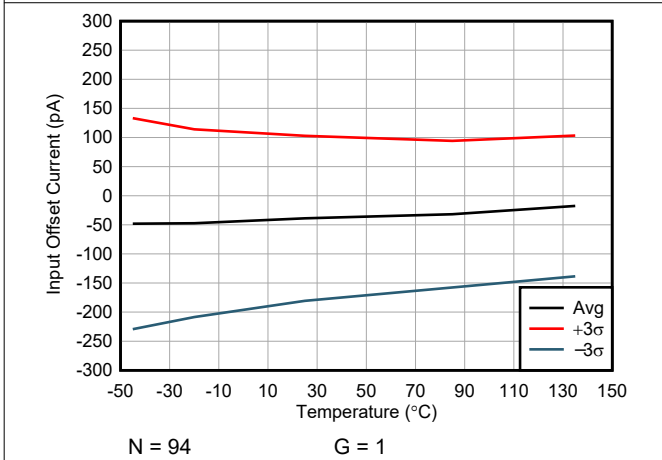
**Figure 7-8. Typical Distribution of Input Bias Current**



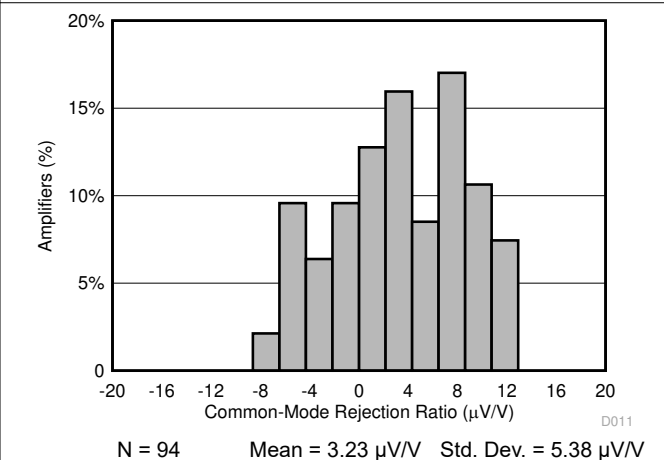
**Figure 7-9. Typical Distribution of Input Offset Current**



**Figure 7-10. Input Bias Current vs Temperature**



**Figure 7-11. Input Offset Current vs Temperature**



**Figure 7-12. Typical CMRR Distribution**

## 7.6 Typical Characteristics (continued)

at  $T_A = 25^\circ\text{C}$ ,  $V_S = \pm 15\text{ V}$ ,  $R_L = 10\text{ k}\Omega$ ,  $V_{REF} = 0\text{ V}$ , and  $G = 1$  (unless otherwise noted)

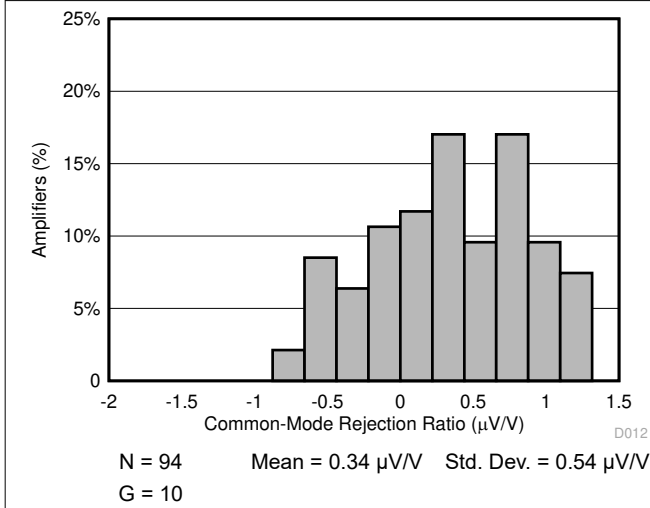


Figure 7-13. Typical CMRR Distribution

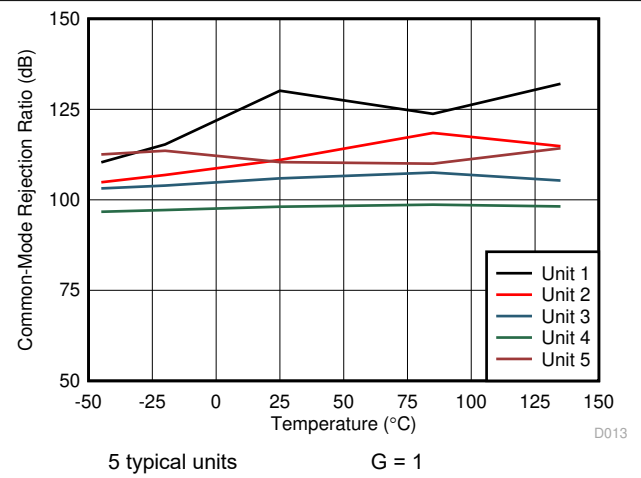


Figure 7-14. CMRR vs Temperature

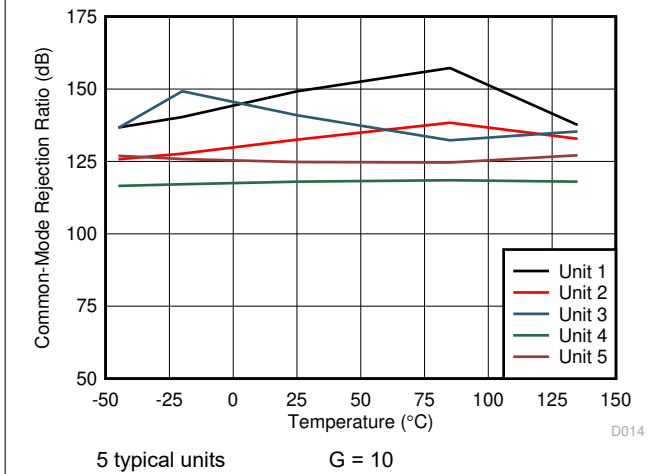


Figure 7-15. CMRR vs Temperature

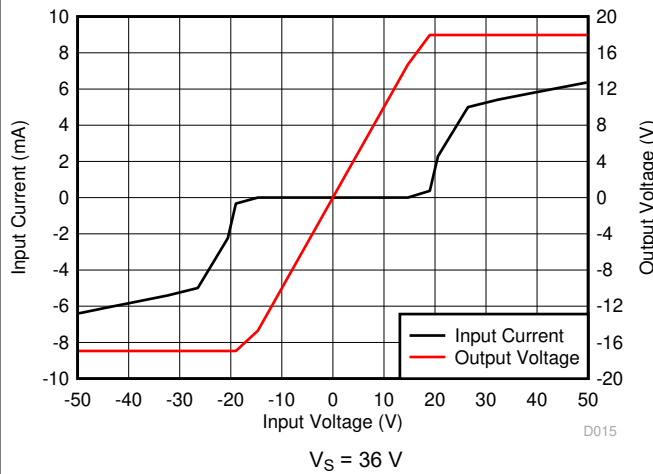


Figure 7-16. Input Current vs Input Overvoltage

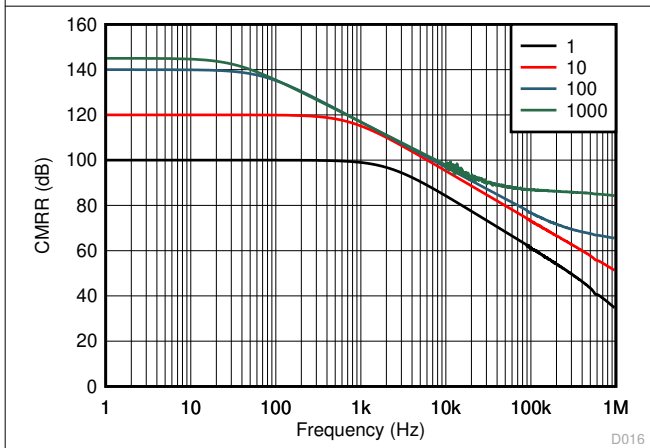


Figure 7-17. CMRR vs Frequency (RTI)

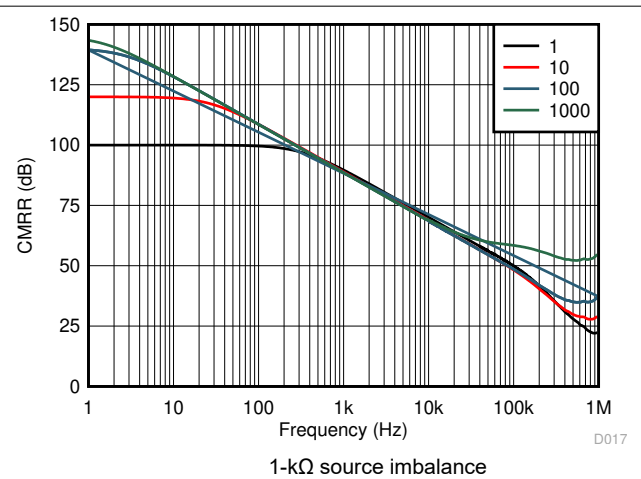


Figure 7-18. CMRR vs Frequency (RTI)

### 7.6 Typical Characteristics (continued)

at  $T_A = 25^\circ\text{C}$ ,  $V_S = \pm 15\text{ V}$ ,  $R_L = 10\text{ k}\Omega$ ,  $V_{REF} = 0\text{ V}$ , and  $G = 1$  (unless otherwise noted)

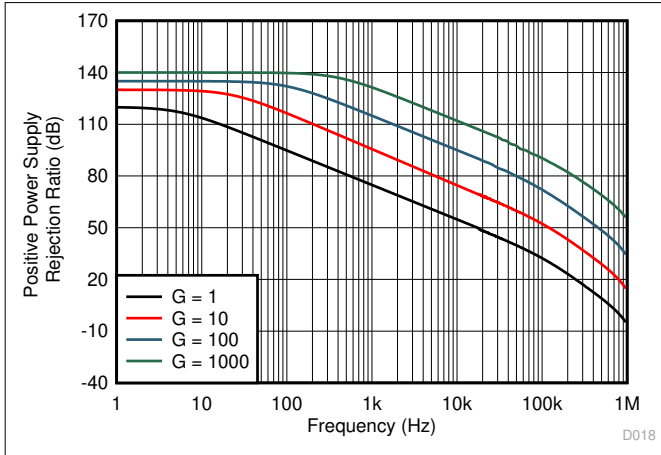


Figure 7-19. Positive PSRR vs Frequency (RTI)

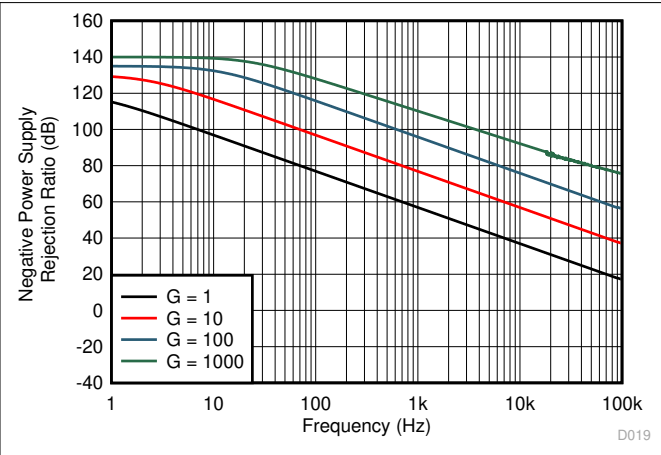


Figure 7-20. Negative PSRR vs Frequency (RTI)

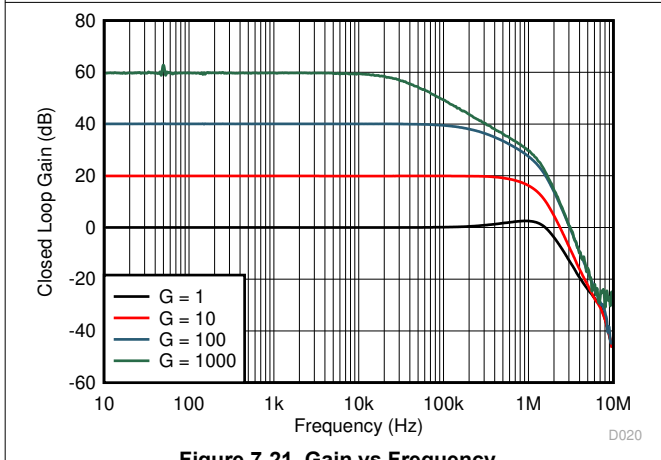


Figure 7-21. Gain vs Frequency

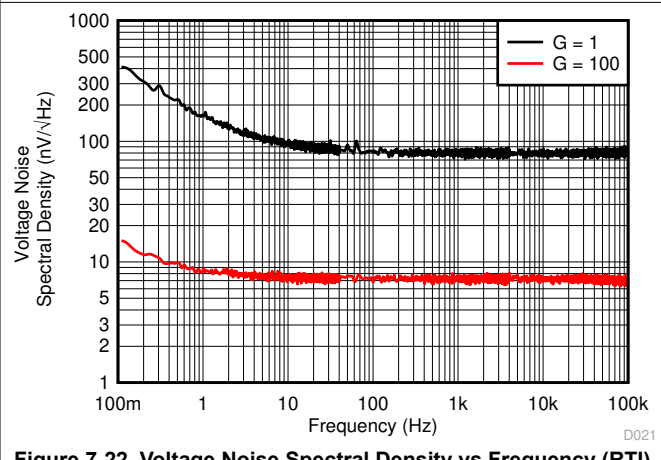


Figure 7-22. Voltage Noise Spectral Density vs Frequency (RTI)

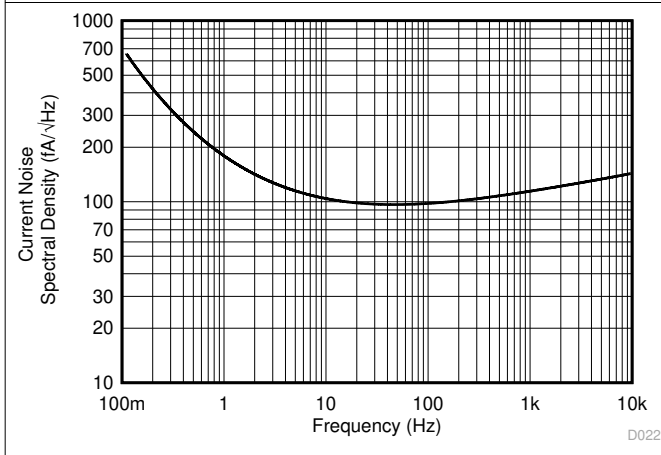


Figure 7-23. Current Noise Spectral Density vs Frequency (RTI)

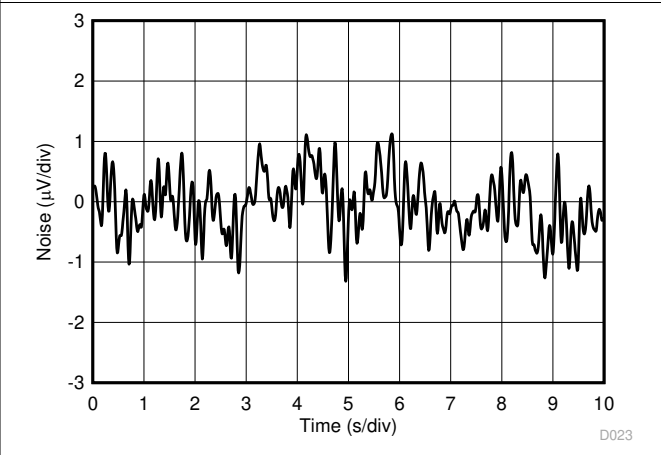


Figure 7-24. 0.1-Hz to 10-Hz RTI Voltage Noise

### 7.6 Typical Characteristics (continued)

at  $T_A = 25^\circ\text{C}$ ,  $V_S = \pm 15\text{ V}$ ,  $R_L = 10\text{ k}\Omega$ ,  $V_{REF} = 0\text{ V}$ , and  $G = 1$  (unless otherwise noted)

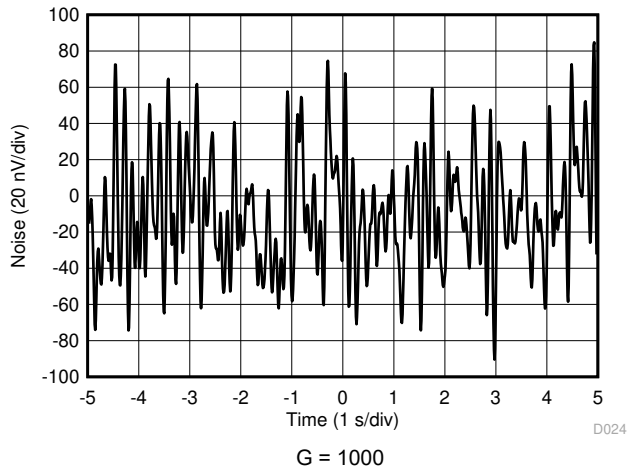


Figure 7-25. 0.1-Hz to 10-Hz RTI Voltage Noise

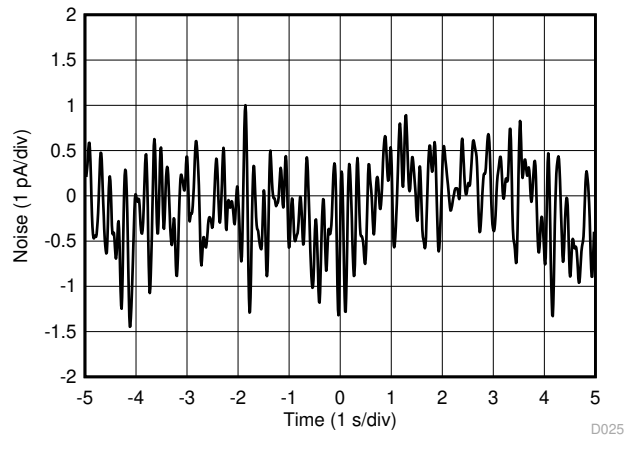


Figure 7-26. 0.1-Hz to 10-Hz RTI Current Noise

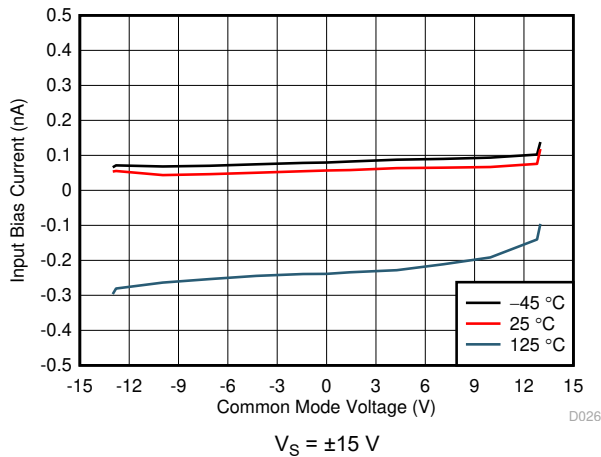


Figure 7-27. Input Bias Current vs Common-Mode Voltage

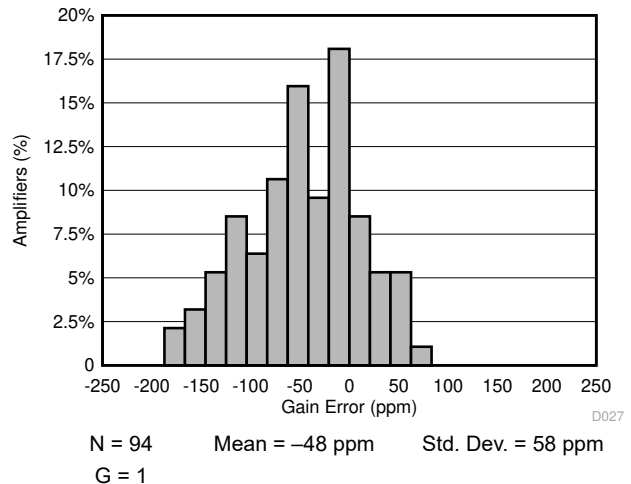


Figure 7-28. Typical Distribution of Gain Error,  $G = 1$

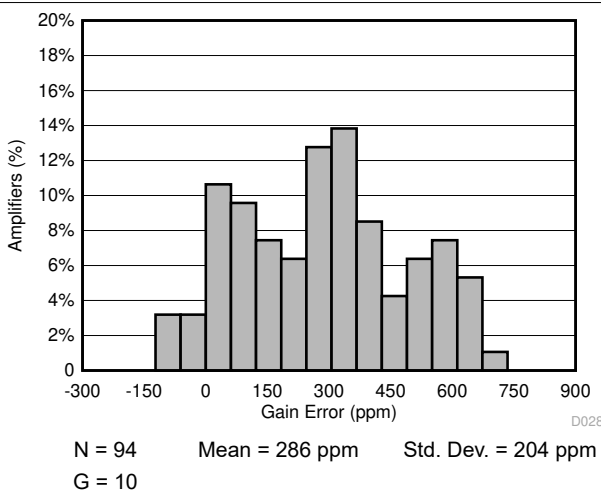


Figure 7-29. Typical Distribution of Gain Error,  $G = 10$

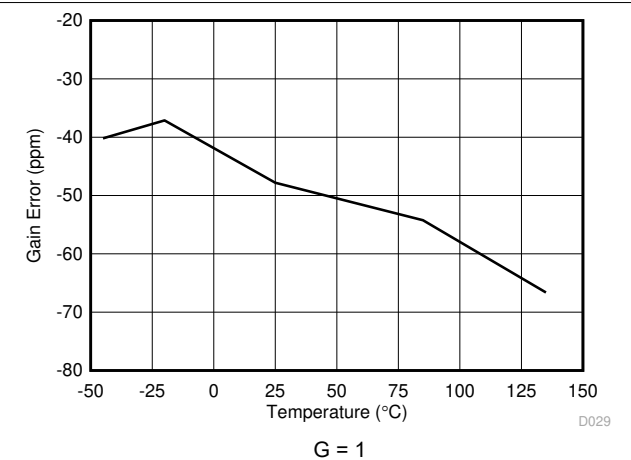
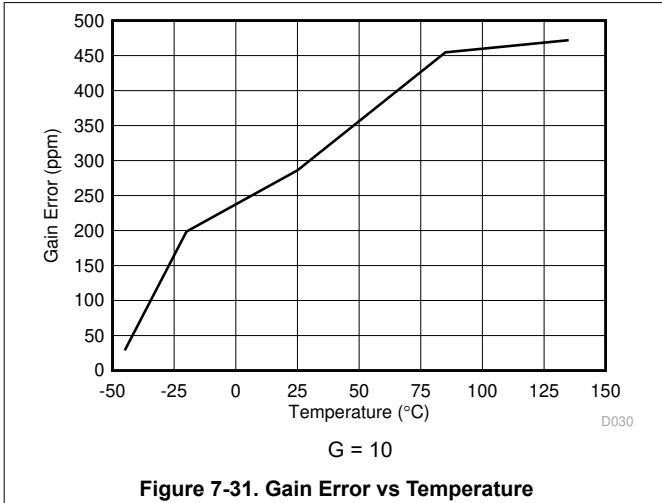


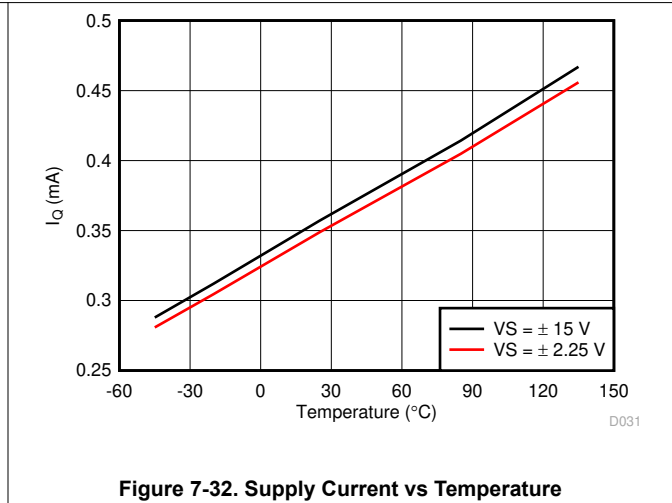
Figure 7-30. Gain Error vs Temperature

### 7.6 Typical Characteristics (continued)

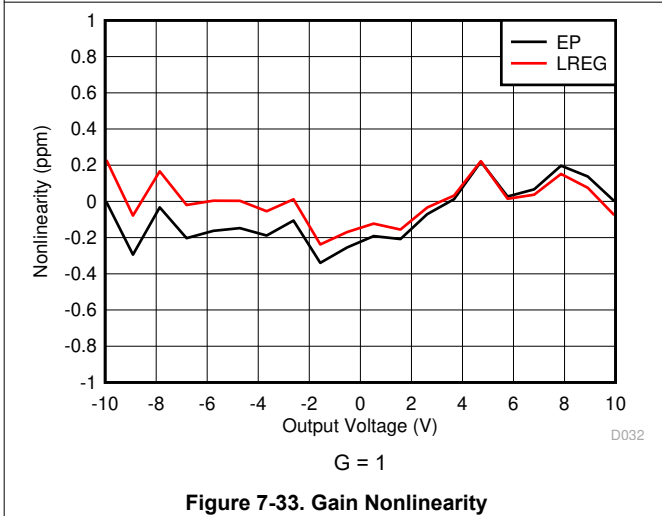
at  $T_A = 25^\circ\text{C}$ ,  $V_S = \pm 15\text{ V}$ ,  $R_L = 10\text{ k}\Omega$ ,  $V_{REF} = 0\text{ V}$ , and  $G = 1$  (unless otherwise noted)



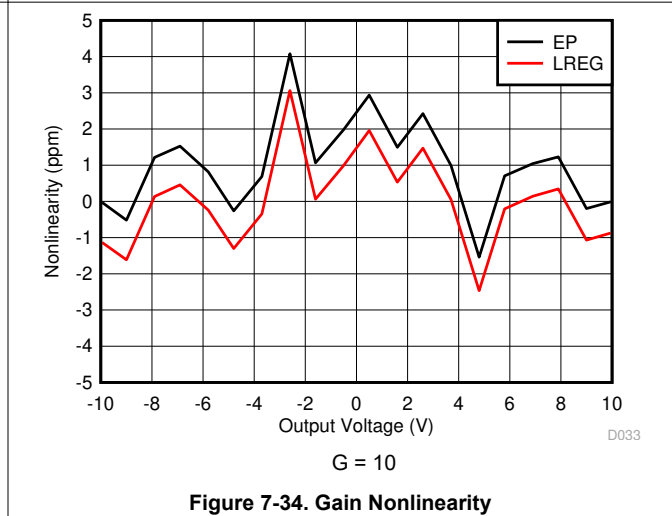
**Figure 7-31. Gain Error vs Temperature**



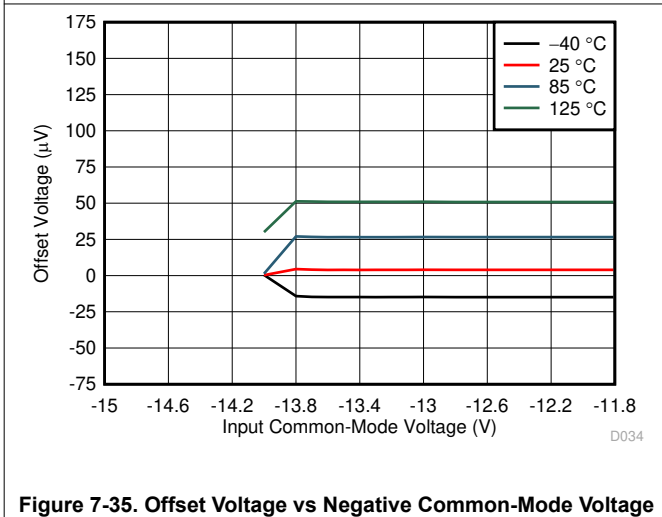
**Figure 7-32. Supply Current vs Temperature**



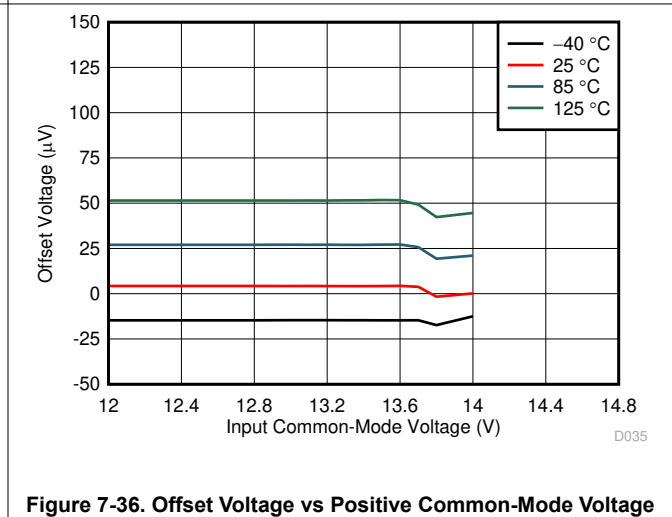
**Figure 7-33. Gain Nonlinearity**



**Figure 7-34. Gain Nonlinearity**



**Figure 7-35. Offset Voltage vs Negative Common-Mode Voltage**



**Figure 7-36. Offset Voltage vs Positive Common-Mode Voltage**

### 7.6 Typical Characteristics (continued)

at  $T_A = 25^\circ\text{C}$ ,  $V_S = \pm 15\text{ V}$ ,  $R_L = 10\text{ k}\Omega$ ,  $V_{REF} = 0\text{ V}$ , and  $G = 1$  (unless otherwise noted)

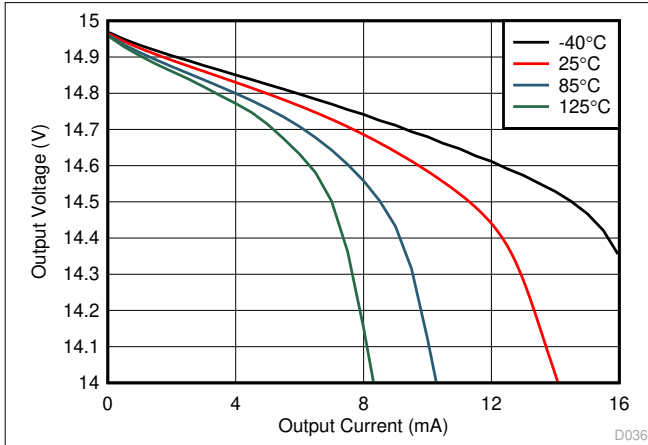


Figure 7-37. Positive Output Voltage Swing vs Output Current

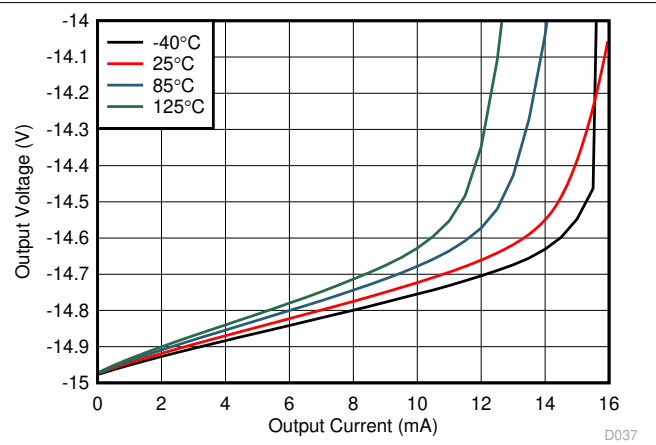


Figure 7-38. Negative Output Voltage Swing vs Output Current

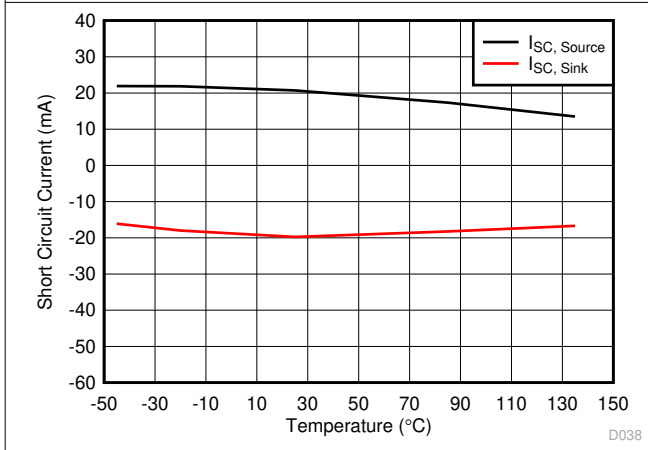


Figure 7-39. Short Circuit Current vs Temperature

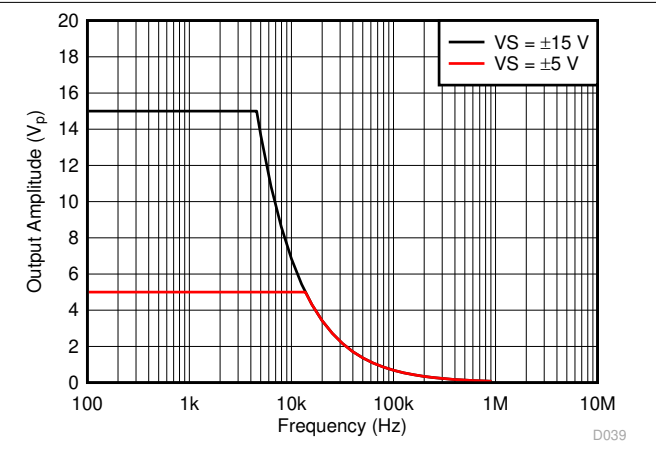


Figure 7-40. Large-Signal Frequency Response

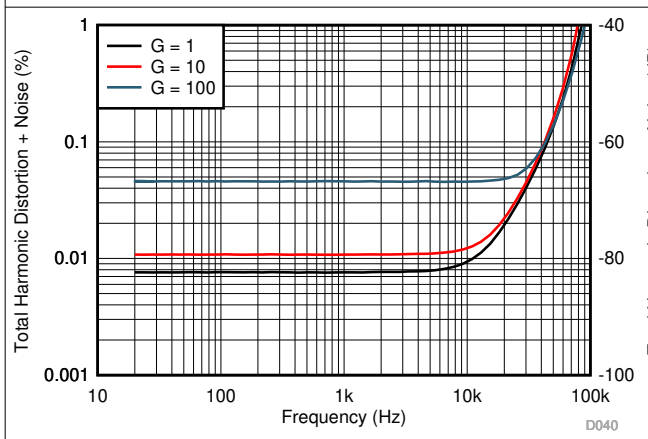


Figure 7-41. THD+N vs Frequency

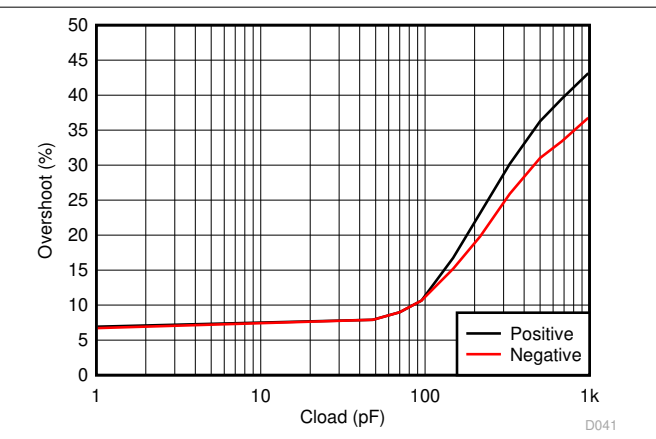
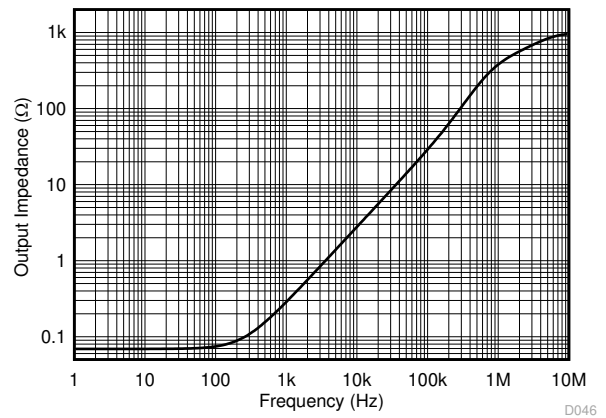
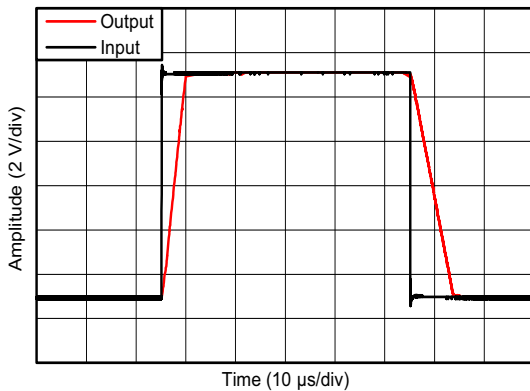
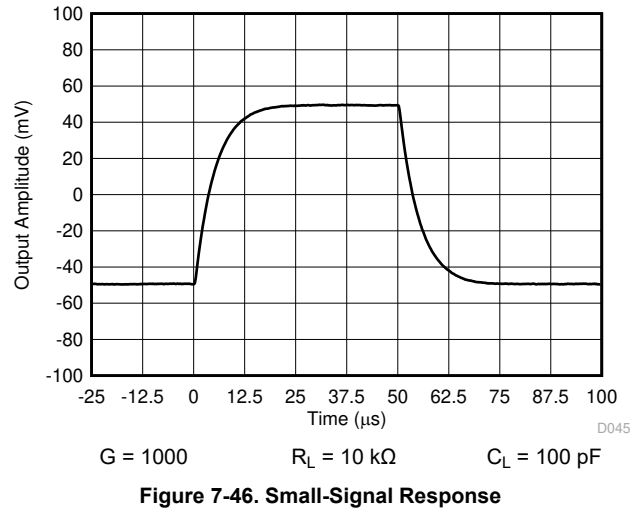
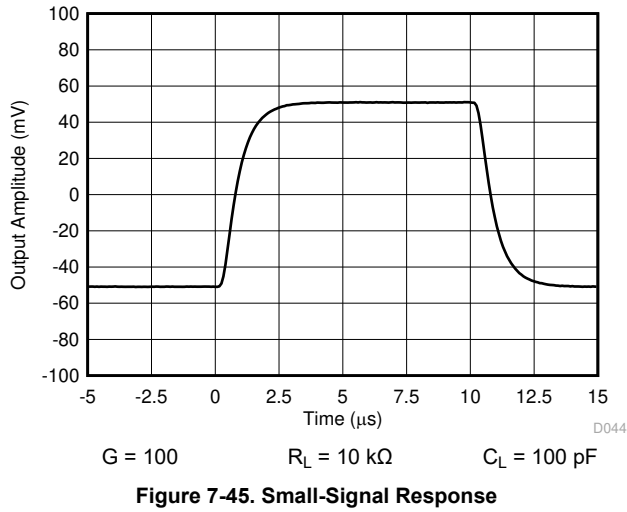
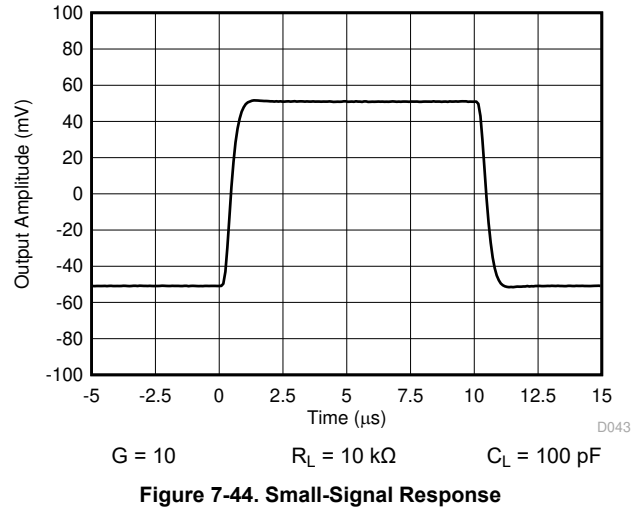
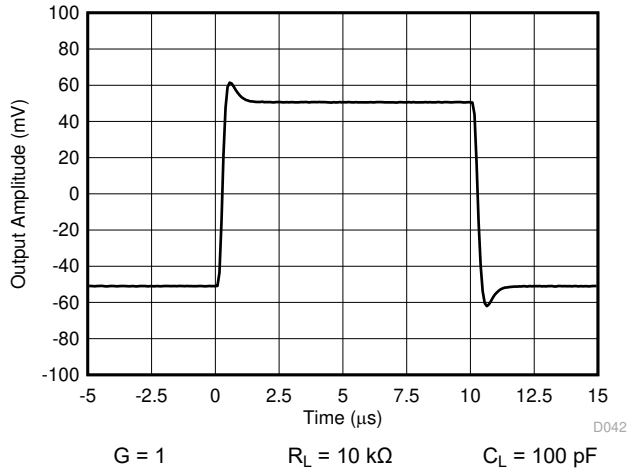


Figure 7-42. Overshoot vs Capacitive Loads

### 7.6 Typical Characteristics (continued)

at  $T_A = 25^\circ\text{C}$ ,  $V_S = \pm 15\text{ V}$ ,  $R_L = 10\text{ k}\Omega$ ,  $V_{REF} = 0\text{ V}$ , and  $G = 1$  (unless otherwise noted)



### 7.6 Typical Characteristics (continued)

at  $T_A = 25^\circ\text{C}$ ,  $V_S = \pm 15\text{ V}$ ,  $R_L = 10\text{ k}\Omega$ ,  $V_{REF} = 0\text{ V}$ , and  $G = 1$  (unless otherwise noted)

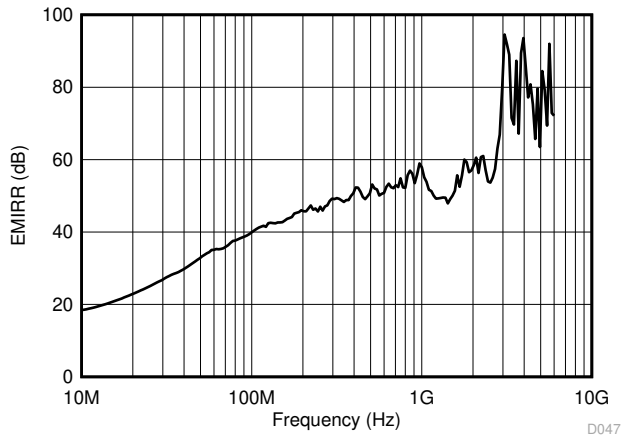


Figure 7-49. Differential-Mode EMI Rejection Ratio

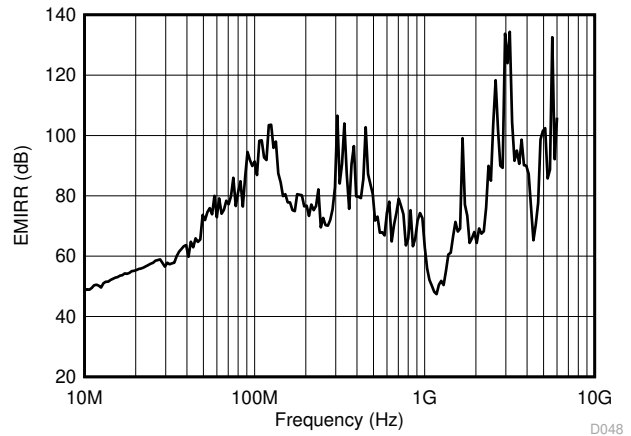


Figure 7-50. Common-Mode EMI Rejection Ratio

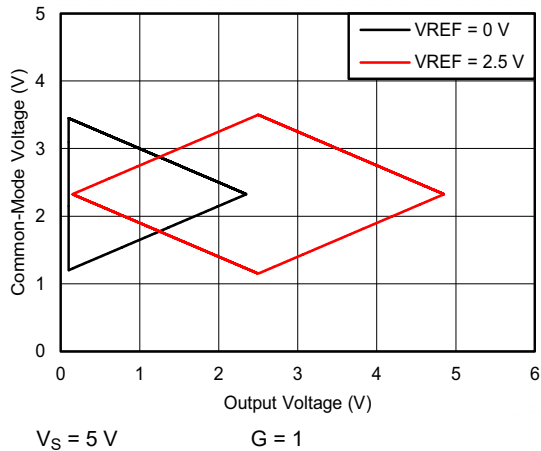


Figure 7-51. Input Common-Mode Voltage vs Output Voltage

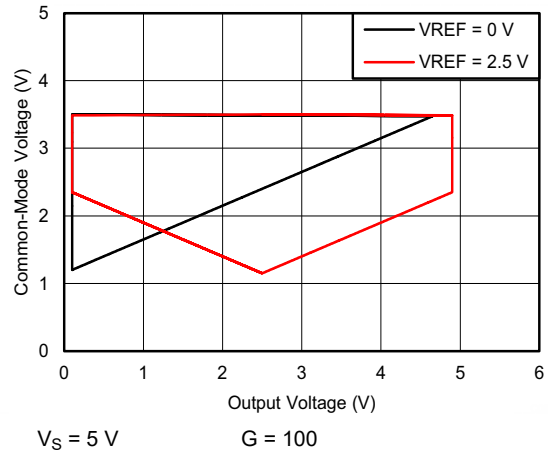


Figure 7-52. Input Common-Mode Voltage vs Output Voltage

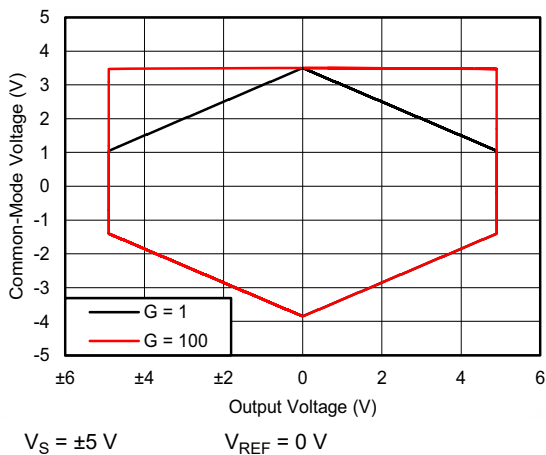


Figure 7-53. Input Common-Mode Voltage vs Output Voltage

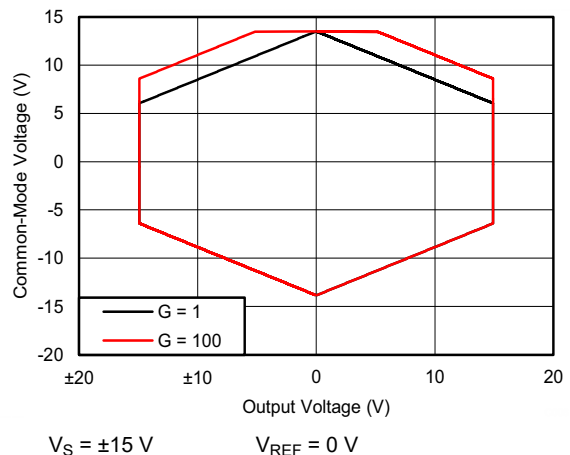


Figure 7-54. Input Common-Mode Voltage vs Output Voltage

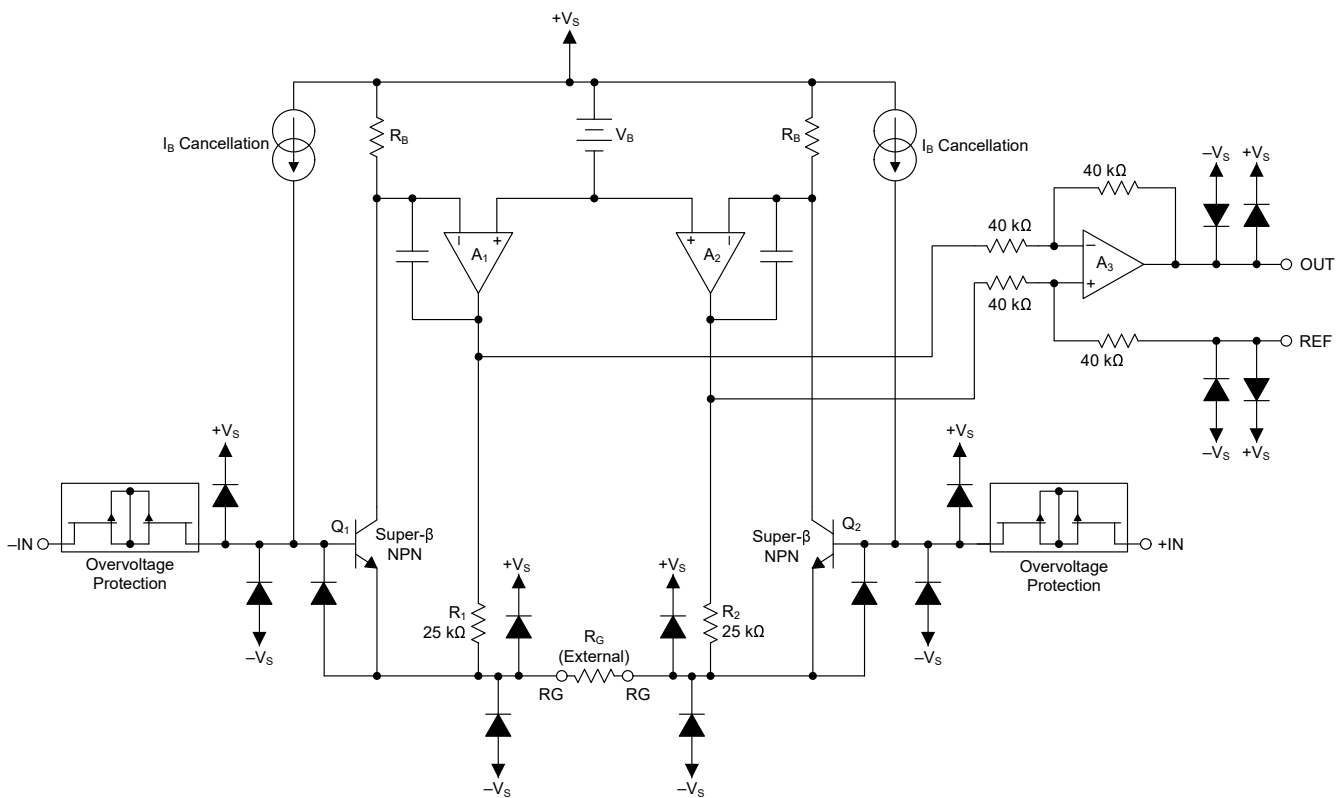
## 8 Detailed Description

### 8.1 Overview

The INA819 is a monolithic precision instrumentation amplifier that incorporates a current-feedback input stage and a four-resistor difference amplifier output stage. The functional block diagram in the next section shows how the differential input voltage is buffered by  $Q_1$  and  $Q_2$  and is forced across  $R_G$ , which causes a signal current to flow through  $R_G$ ,  $R_1$ , and  $R_2$ . The output difference amplifier,  $A_3$ , removes the common-mode component of the input signal and refers the output signal to the REF pin. The  $V_{BE}$  and voltage drop across  $R_1$  and  $R_2$  produce output voltages on  $A_1$  and  $A_2$  that are approximately 0.8 V lower than the input voltages.

Each input is protected by two field-effect transistors (FETs) that provide a low series resistance under normal signal conditions, and preserve excellent noise performance. When excessive voltage is applied, these transistors limit input current to approximately 8 mA.

### 8.2 Functional Block Diagram



### 8.3 Feature Description

#### 8.3.1 Setting the Gain

Figure 8-1 shows that the gain of the INA819 is set by a single external resistor ( $R_G$ ) connected between the RG pins (pins 1 and 8).

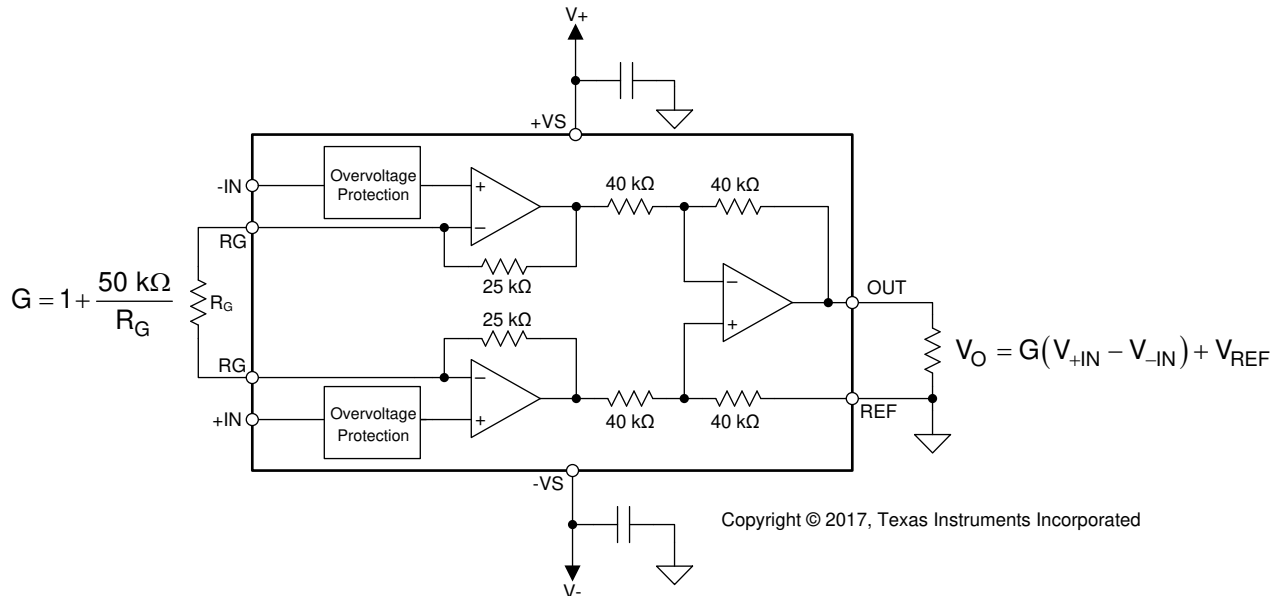


Figure 8-1. Simplified Diagram of the INA819 With Gain and Output Equations

The value of  $R_G$  is selected according to Equation 1:

$$G = 1 + \frac{50 \text{ k}\Omega}{R_G} \tag{1}$$

Table 8-1 lists several commonly used gains and resistor values. The 50-kΩ term in Equation 1 is a result of the sum of the two internal 25-kΩ feedback resistors. These on-chip resistors are laser-trimmed to accurate absolute values. The accuracy and temperature coefficients of these resistors are included in the gain accuracy and drift specifications of the INA819. As shown in Figure 8-1 and explained in more details in Section 11, make sure to connect low-ESR, 0.1-μF ceramic bypass capacitors between each supply pin and ground that are placed as close to the device as possible.

Table 8-1. Commonly Used Gains and Resistor Values

DESIRED GAIN	$R_G$ (Ω)	NEAREST 1% $R_G$ (Ω)
1	NC	NC
2	50 k	49.9 k
5	12.5 k	12.4 k
10	5.556 k	5.49 k
20	2.632 k	2.61 k
50	1.02 k	1.02 k
100	505.1	511
200	251.3	249
500	100.2	100
1000	50.05	49.9

### 8.3.1.1 Gain Drift

The stability and temperature drift of the external gain setting resistor ( $R_G$ ) also affects gain. The contribution of  $R_G$  to gain accuracy and drift is determined from Equation 1.

The best gain drift of 5 ppm/°C (maximum) is achieved when the INA819 uses  $G = 1$  without  $R_G$  connected. In this case, gain drift is limited by the mismatch of the temperature coefficient of the integrated 40-kΩ resistors in the differential amplifier ( $A_3$ ). At gains greater than 1, gain drift increases as a result of the individual drift of the 25-kΩ resistors in the feedback of  $A_1$  and  $A_2$ , relative to the drift of the external gain resistor ( $R_G$ .) The low temperature coefficient of the internal feedback resistors improves the overall temperature stability of applications using gains greater than 1 V/V over alternate solutions.

Low resistor values required for high gain make wiring resistance an important consideration. Sockets add to the wiring resistance and contribute additional gain error (such as a possible unstable gain error) at gains of approximately 100 or greater. To maintain stability, avoid parasitic capacitance of more than a few picofarads at  $R_G$  connections. Careful matching of any parasitics on the  $R_G$  pins maintains optimal CMRR over frequency; see Figure 7-17.

### 8.3.2 EMI Rejection

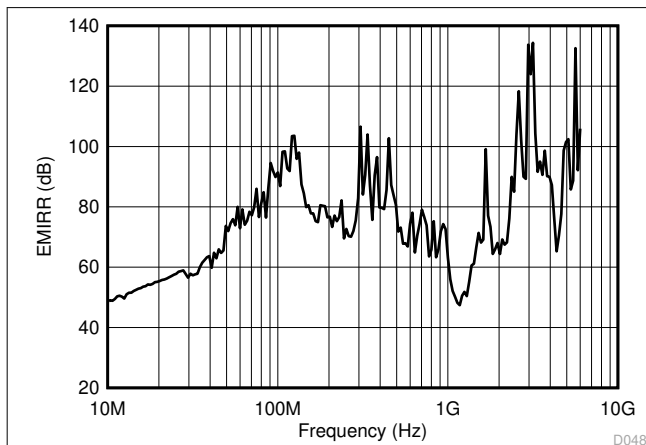
Texas Instruments developed a method to accurately measure the immunity of an amplifier over a broad frequency spectrum extending from 10 MHz to 6 GHz. This method uses an EMI rejection ratio (EMIRR) to quantify the ability of the INA819 to reject EMI. The offset resulting from an input EMI signal is calculated using Equation 2:

$$\Delta V_{OS} = \left( \frac{V_{RF\_PEAK}^2}{100 \text{ mV}_p} \right) \cdot 10^{-\left( \frac{EMIRR \text{ (dB)}}{20} \right)} \quad (2)$$

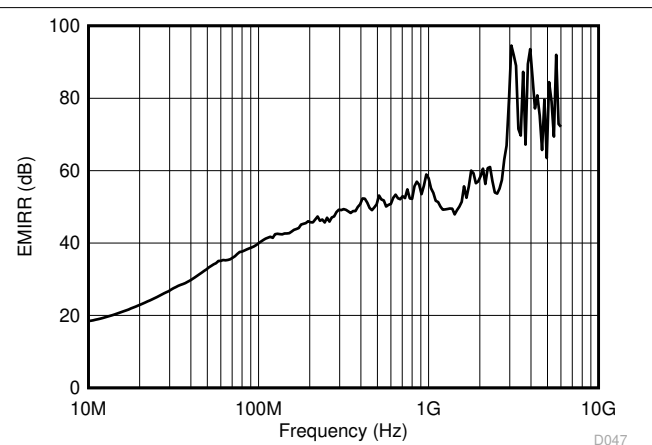
where

- $V_{RF\_PEAK}$  is the peak amplitude of the input EMI signal.

Figure 8-2 and Figure 8-3 show the INA819 EMIRR graph for differential and common-mode EMI rejection across this frequency range. Table 8-2 lists the EMIRR values for the INA819 at frequencies commonly encountered in real-world applications. Applications listed in Table 8-2 are centered on or operated near the frequency shown. Depending on the end-system requirements, additional EMI filters may be required near the signal inputs of the system. Incorporating known good practices such as using short traces, low-pass filters, and damping resistors combined with parallel and shielded signal routing may be required.



**Figure 8-2. Common-Mode EMIRR Testing**



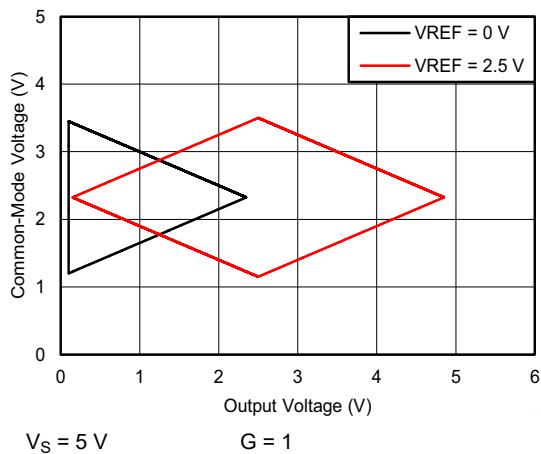
**Figure 8-3. Differential Mode EMIRR Testing**

**Table 8-2. INA819 EMIRR for Frequencies of Interest**

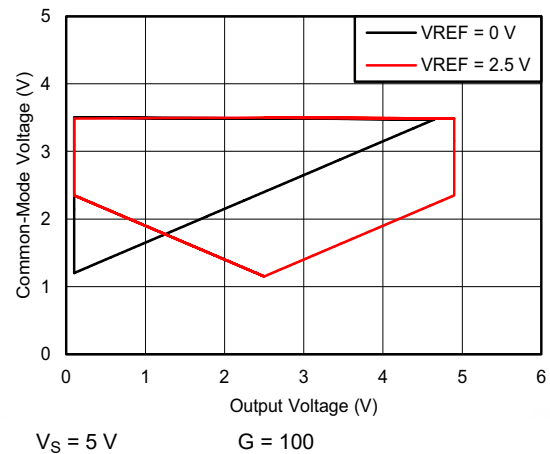
FREQUENCY	APPLICATION OR ALLOCATION	DIFFERENTIAL EMIRR	COMMON-MODE EMIRR
400 MHz	Mobile radio, mobile satellite, space operation, weather, radar, ultrahigh-frequency (UHF) applications	52 dB	80 dB
900 MHz	Global system for mobile communications (GSM) applications, radio communication, navigation, GPS (up to 1.6 GHz), GSM, aeronautical mobile, UHF applications	55 dB	71 dB
1.8 GHz	GSM applications, mobile personal communications, broadband, satellite, L-band (1 GHz to 2 GHz)	58 dB	73 dB
2.4 GHz	802.11b, 802.11g, 802.11n, Bluetooth®, mobile personal communications, industrial, scientific and medical (ISM) radio band, amateur radio and satellite, S-band (2 GHz to 4 GHz)	59 dB	95 dB
3.6 GHz	Radiolocation, aero communication and navigation, satellite, mobile, S-band	78 dB	96 dB
5 GHz	802.11a, 802.11n, aero communication and navigation, mobile communication, space and satellite operation, C-band (4 GHz to 8 GHz)	70 dB	100 dB

**8.3.3 Input Common-Mode Range**

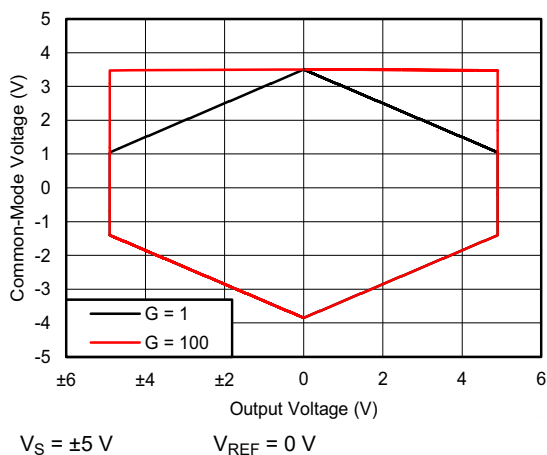
The linear input voltage range of the INA819 input circuitry extends within 1.5 volts (typical) of both power supplies and maintains excellent common-mode rejection throughout this range. The common-mode range for the most common operating conditions are shown in [Figure 8-4](#) to [Figure 8-7](#). The common-mode range for other operating conditions is best calculated using the [Analog Engineers Calculator](#).



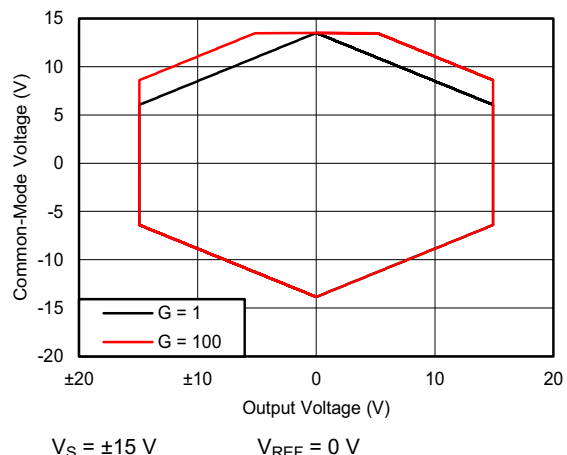
**Figure 8-4. Input Common-Mode Voltage vs Output Voltage**



**Figure 8-5. Input Common-Mode Voltage vs Output Voltage**



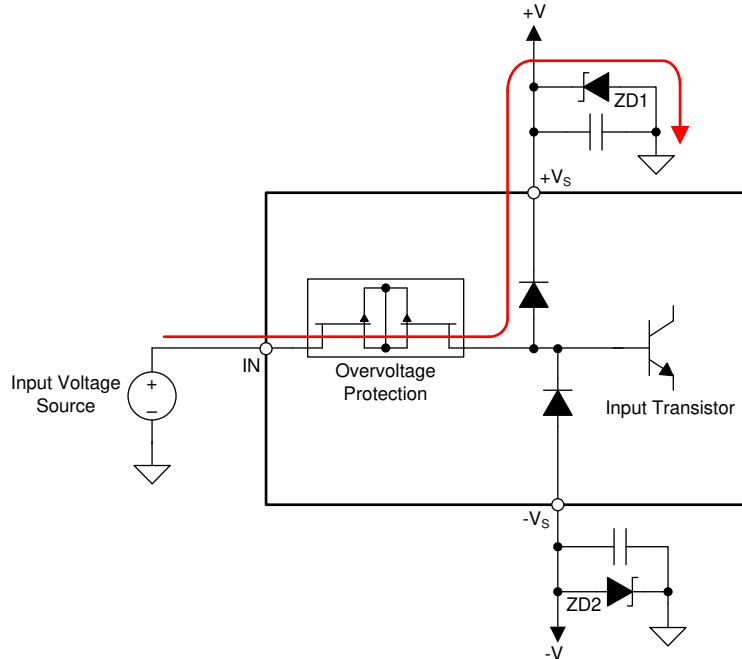
**Figure 8-6. Input Common-Mode Voltage vs Output Voltage**



**Figure 8-7. Input Common-Mode Voltage vs Output Voltage**

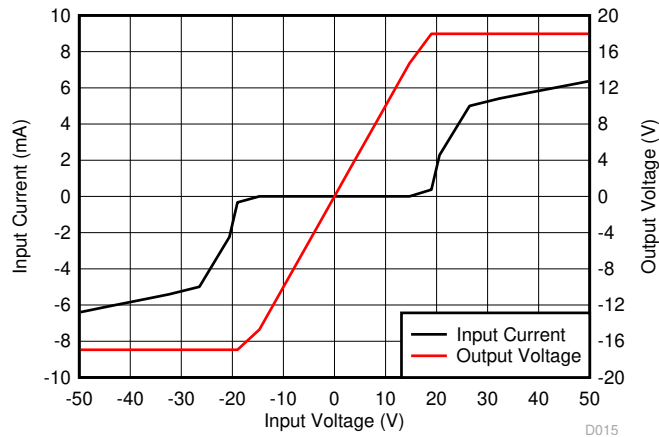
### 8.3.4 Input Protection

The inputs of the INA819 device are individually protected for voltages up to  $\pm 60$  V. For example, a condition of  $-60$  V on one input and  $+60$  V on the other input does not cause damage. Internal circuitry on each input provides low series impedance under normal signal conditions. If the input is overloaded, the protection circuitry limits the input current to a value of approximately 8 mA.



**Figure 8-8. Input Current Path During an Overvoltage Condition**

During an input overvoltage condition, current flows through the input protection diodes into the power supplies; see Figure 8-8. If the power supplies are unable to sink current, then Zener diode clamps (ZD1 and ZD2 in Figure 8-8) must be placed on the power supplies to provide a current pathway to ground. Figure 8-9 shows the input current for input voltages from  $-50$  V to  $50$  V when the INA819 is powered by  $\pm 15$ -V supplies.



**Figure 8-9. Input Current vs Input Overvoltage**

### 8.3.5 Operating Voltage

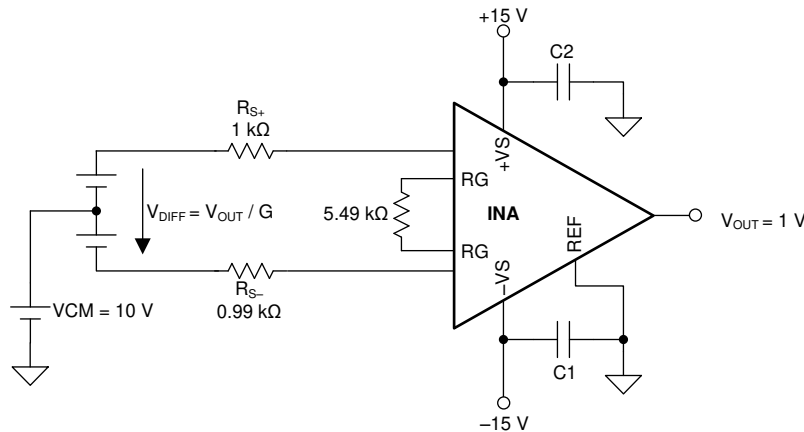
The INA819 operates over a power-supply range of 4.5 V to 36 V ( $\pm 2.25$  V to  $\pm 18$  V).

#### CAUTION

Supply voltages higher than 40 V ( $\pm 20$  V) can permanently damage the device. Parameters that vary over supply voltage or temperature are shown in [Section 7.6](#).

### 8.3.6 Error Sources

Most modern signal-conditioning systems calibrate errors at room temperature. However, calibration of errors that result from a change in temperature is normally difficult and costly. Therefore, minimize these errors by choosing high-precision components, such as the INA819, that have improved specifications in critical areas that impact the precision of the overall system. [Figure 8-10](#) shows an example application.



**Figure 8-10. Example Application with  $G = 10$  V/V and 1-V Output Voltage**

Resistor-adjustable devices (such as the INA819) show the lowest gain error in  $G = 1$  because of the inherently well-matched drift of the internal resistors of the differential amplifier. At gains greater than 1 (for instance,  $G = 10$  V/V or  $G = 100$  V/V), the gain error becomes a significant error source because of the contribution of the resistor drift of the 25-k $\Omega$  feedback resistors in conjunction with the external gain resistor. Except for very high gain applications, the gain drift is by far the largest error contributor compared to other drift errors, such as offset drift.

The INA819 offers excellent gain error over temperature for both  $G > 1$  and  $G = 1$  (no external gain resistor). [Table 8-4](#) summarizes the major error sources in common INA applications and compares the three cases of  $G = 1$  (no external resistor) and  $G = 10$  (5.49-k $\Omega$  external resistor) and  $G = 100$  (511- $\Omega$  external resistor). All calculations are assuming an output voltage of  $V_{OUT} = 1$  V. Thus, the input signal  $V_{DIFF}$  (given by  $V_{DIFF} = V_{OUT}/G$ ) exhibits smaller and smaller amplitudes with increasing gain  $G$ . In this example,  $V_{DIFF} = 1$  mV at  $G = 1000$ . All calculations refer the error to the input for easy comparison and system evaluation. As [Table 8-4](#) shows, errors generated by the input stage (such as input offset voltage) are more dominant at higher gain, while the effects of output stage are suppressed because they are divided by the gain when referring them back to the input. The gain error and gain drift error are much more significant for gains greater than 1 because of the contribution of the resistor drift of the 25-k $\Omega$  feedback resistors in conjunction with the external gain resistor. In most applications, static errors (absolute accuracy errors) can readily be removed during calibration in production, while the drift errors are the key factors limiting overall system performance.

**Table 8-3. System Specifications for Error Calculation**

QUANTITY	VALUE	UNIT
V <sub>OUT</sub>	1	V
V <sub>CM</sub>	10	V
V <sub>S</sub>	1	V
R <sub>S+</sub>	1000	Ω
R <sub>S-</sub>	999	Ω
RG tolerance	0.01	%
RG drift	10	ppm/°C
Temperature range upper limit	105	°C

**Table 8-4. Error Calculation**

ERROR SOURCE	ERROR CALCULATION	INA819 VALUES				
		SPECIFICATION	UNIT	G = 1 ERROR (ppm)	G = 100 ERROR (ppm)	G = 1000 ERROR (ppm)
<b>ABSOLUTE ACCURACY AT 25°C</b>						
Input offset voltage	V <sub>OSI</sub> / V <sub>DIFF</sub>	35	μV	35	350	3500
Output offset voltage	V <sub>OSO</sub> / (G × V <sub>DIFF</sub> )	300	μV	300	300	300
Input offset current	I <sub>OS</sub> × maximum (R <sub>S+</sub> , R <sub>S-</sub> ) / V <sub>DIFF</sub>	0.5	nA	1	5	50
CMRR (min)	V <sub>CM</sub> / (10 <sup>CMRR/20</sup> × V <sub>DIFF</sub> )	90 (G = 1), 110 (G = 10), 130 (G = 100)	dB	316	316	316
PSRR (min)	(V <sub>CC</sub> - V <sub>S</sub> ) / (10 <sup>PSRR/20</sup> × V <sub>DIFF</sub> )	110 (G = 1), 114 (G = 10), 130 (G = 100)	dB	3	20	32
Gain error from INA (max)	GE(%) × 10 <sup>4</sup>	0.02 (G = 1), 0.15 (G = 10, 100)	%	200	1500	1500
Gain error from external resistor RG (max)	GE(%) × 10 <sup>4</sup>	0.01	%	100	100	100
Total absolute accuracy error (ppm) at 25°C, worst case	sum of all errors	—	—	955	2591	5798
Total absolute accuracy error (ppm) at 25°C, average	rms sum of all errors	—	—	491	1604	3835
<b>DRIFT TO 105°C</b>						
Gain drift from INA (max)	GTC × (T <sub>A</sub> - 25)	5 (G = 1), 35 (G = 10, 100)	ppm/°C	400	2800	2800
Gain drift from external resistor RG (max)	GTC × (T <sub>A</sub> - 25)	10	ppm/°C	800	800	800
Input offset voltage drift (max)	(V <sub>OSI_TC</sub> / V <sub>DIFF</sub> ) × (T <sub>A</sub> - 25)	0.4	μV/°C	32	320	3200
Output offset voltage drift	[V <sub>OSO_TC</sub> / (G × V <sub>DIFF</sub> )] × (T <sub>A</sub> - 25)	5	μV/°C	400	400	400
Offset current drift	I <sub>OS_TC</sub> × maximum (R <sub>S+</sub> , R <sub>S-</sub> ) × (T <sub>A</sub> - 25) / V <sub>DIFF</sub>	20	pA/°C	2	16	160
Total drift error to 105°C (ppm), worst case	sum of all errors	—	—	1634	4336	7360
Total drift error to 105°C (ppm), typical	rms sum of all errors	—	—	980	2957	4348
<b>RESOLUTION</b>						
Gain nonlinearity		10 (G = 1, 10), 15 (G = 100)	ppm of FS	10	10	15
Voltage noise (at 1 kHz)	$\sqrt{BW} \times \sqrt{(e_{NI})^2 + \left(\frac{e_{NO}}{G}\right)^2} \times \frac{6}{V_{DIFF}}$	e <sub>NI</sub> = 8, e <sub>NO</sub> = 90	μV <sub>PP</sub>	1204	1070	3941
Current noise (at 1kHz)	I <sub>N</sub> × maximum (R <sub>S+</sub> , R <sub>S-</sub> ) × √BW / V <sub>DIFF</sub>	0.13	pA/√Hz	0.3	2	11
Total resolution error (ppm), worst case	sum of all errors	—	—	1214	1080	3956
Total resolution error (ppm), typical	rms sum of all errors	—	—	1204	1070	3941
<b>TOTAL ERROR</b>						
Total error (ppm), worst case	sum of all errors	—	—	3802	8007	17113
Total error (ppm), typical	rms sum of all errors	—	—	1628	3530	7010

## 8.4 Device Functional Modes

The INA819 has a single functional mode and operates when the power-supply voltage is greater than 4.5 V ( $\pm 2.25$  V). The maximum power-supply voltage for the INA819 is 36 V ( $\pm 18$  V.)

## 9 Application and Implementation

### Note

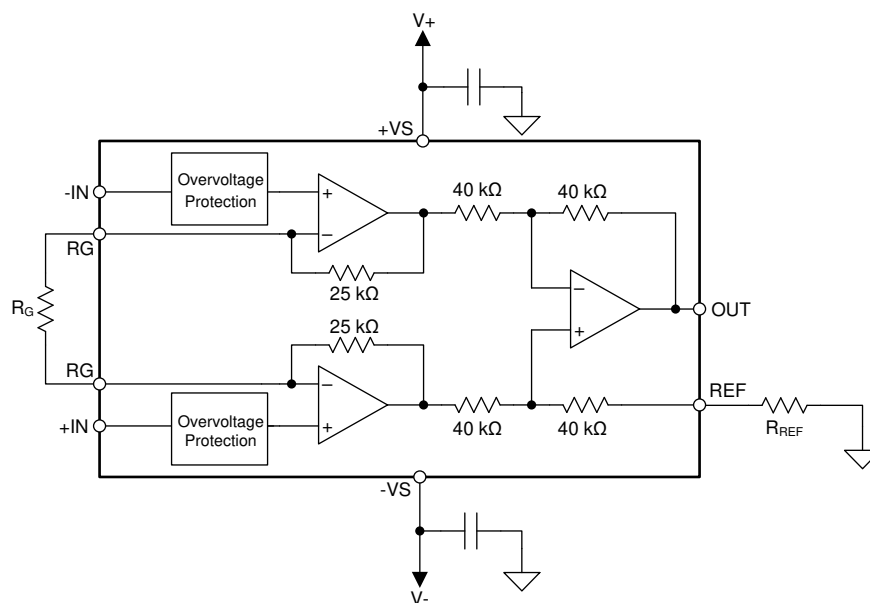
Information in the following applications sections is not part of the TI component specification, and TI does not warrant its accuracy or completeness. TI's customers are responsible for determining suitability of components for their purposes, as well as validating and testing their design implementation to confirm system functionality.

### 9.1 Application Information

#### 9.1.1 Reference Pin

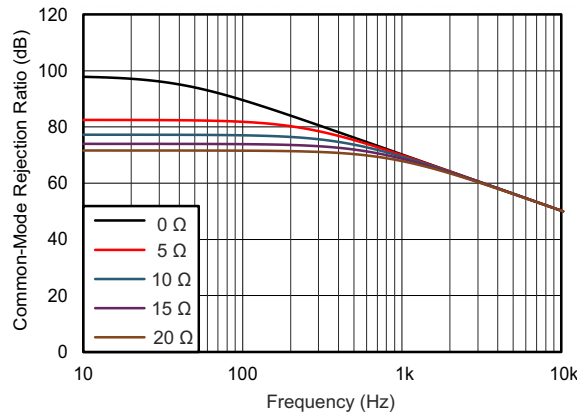
The output voltage of the INA819 is developed with respect to the voltage on the reference pin (REF.) Often, in dual-supply operation, REF (pin 6) is connected to the low-impedance system ground. In single-supply operation, offsetting the output signal to a precise midsupply level is useful (for example, 2.5 V in a 5-V supply environment). To accomplish this level shift, a voltage source must be connected to the REF pin to level-shift the output so that the INA819 drives a single-supply analog-to-digital converter (ADC).

The voltage source applied to the reference pin must have a low output impedance. As shown in [Figure 9-1](#), any resistance at the reference pin (shown as  $R_{REF}$  in [Figure 9-1](#)) is in series with an internal 40-k $\Omega$  resistor.



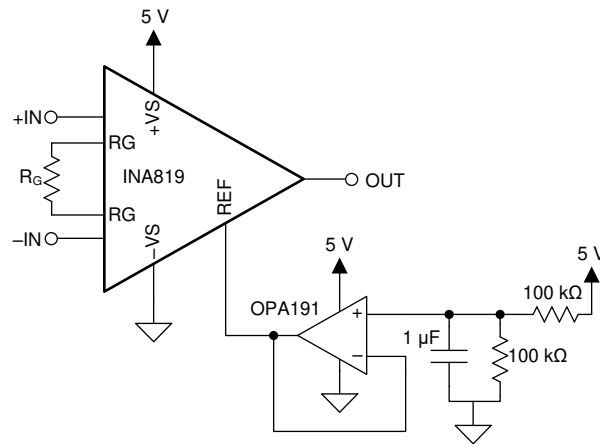
**Figure 9-1. Parasitic Resistance Shown at the Reference Pin**

The parasitic resistance at the reference pin ( $R_{REF}$ ) creates an imbalance in the four resistors of the internal difference amplifier that results in a degraded common-mode rejection ratio (CMRR). Figure 9-2 shows the degradation in CMRR of the INA819 as a result of increased resistance at the reference pin. For the best performance, keep the source impedance to the REF pin ( $R_{REF}$ ) less than  $5\ \Omega$ .



**Figure 9-2. The Effect of Increasing Resistance at the Reference Pin**

Voltage reference devices are an excellent option for providing a low-impedance voltage source for the reference pin. However, if a resistor voltage divider generates a reference voltage, the divider must be buffered by an op amp, as Figure 9-3 shows, to avoid CMRR degradation.



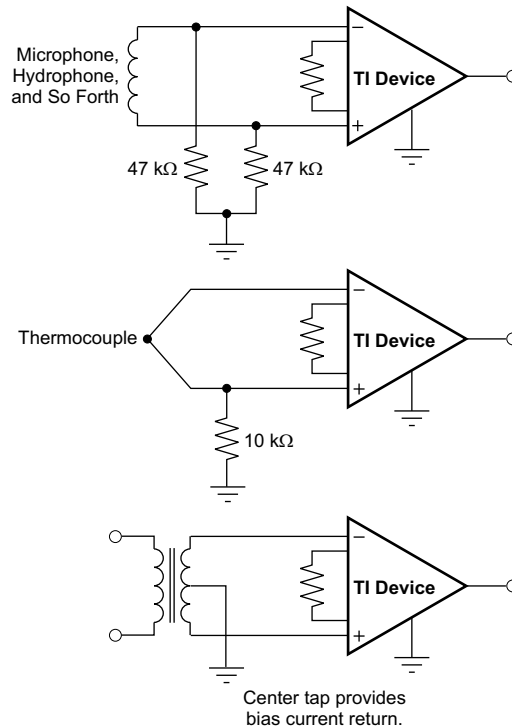
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**Figure 9-3. Using an Op Amp to Buffer Reference Voltages**

### 9.1.2 Input Bias Current Return Path

The input impedance of the INA819 is extremely high—approximately 100 G $\Omega$ . However, a path must be provided for the input bias current of both inputs. This input bias current is typically 150 pA. High input impedance means that this input bias current changes very little with varying input voltage.

For proper operation, input circuitry must provide a path for input bias current. [Figure 9-4](#) shows various provisions for an input bias current path. Without a bias current path, the inputs float to a potential that exceeds the common-mode range of the INA819, and the input amplifiers saturate. If the differential source resistance is low, the bias current return path can connect to one input (as shown in the thermocouple example in [Figure 9-4](#)). With a higher source impedance, using two equal resistors provides a balanced input with possible advantages of a lower input offset voltage as a result of bias current and better high-frequency common-mode rejection.



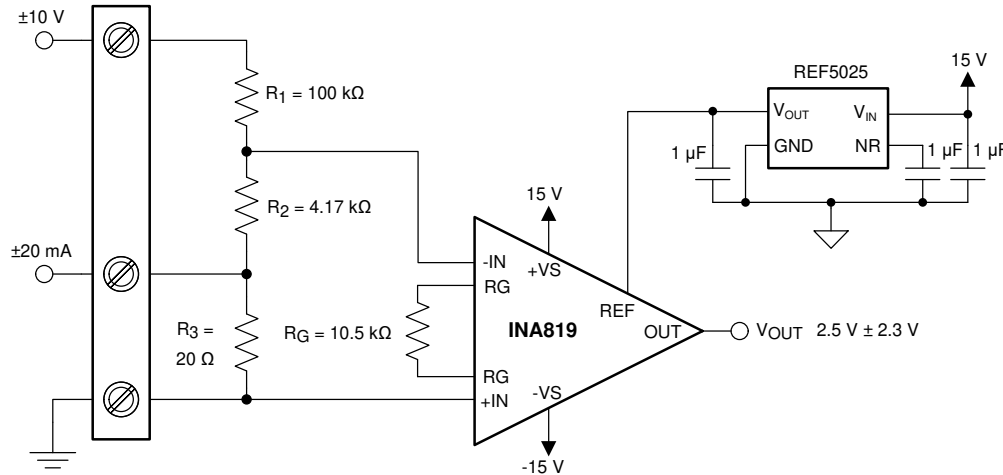
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**Figure 9-4. Providing an Input Common-Mode Current Path**

## 9.2 Typical Applications

### 9.2.1 Three-Pin Programmable Logic Controller (PLC)

Figure 9-5 shows a three-pin programmable-logic controller (PLC) design for the INA819. This PLC reference design accepts inputs of  $\pm 10$  V or  $\pm 20$  mA. The output is a single-ended voltage of  $2.5$  V  $\pm 2.3$  V (or 200 mV to 4.8 V). Many PLCs typically have these input and output ranges.



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**Figure 9-5. PLC Input ( $\pm 10$  V, 4 mA to 20 mA)**

#### 9.2.1.1 Design Requirements

For this application, the design requirements are as follows:

- 4-mA to 20-mA input with less than 20- $\Omega$  burden
- $\pm 20$ -mA input with less than 20- $\Omega$  burden
- $\pm 10$ -V input with impedance of approximately 100 k $\Omega$
- Maximum 4-mA to 20-mA or  $\pm 20$ -mA burden voltage equal to  $\pm 0.4$  V
- Output range within 0 V to 5 V

#### 9.2.1.2 Detailed Design Procedure

There are two modes of operation for the circuit shown in Figure 9-5: current input and voltage input. This design requires  $R_1 \gg R_2 \gg R_3$ . Given this relationship, Equation 3 calculates the current input mode transfer function.

$$V_{\text{OUT-I}} = V_{\text{D}} \times G + V_{\text{REF}} = -(I_{\text{IN}} \times R_3) \times G + V_{\text{REF}} \quad (3)$$

where

- $G$  represents the gain of the instrumentation amplifier.
- $V_{\text{D}}$  represents the differential voltage at the INA819 inputs.
- $V_{\text{REF}}$  is the voltage at the INA819 REF pin.
- $I_{\text{IN}}$  is the input current.

Equation 4 shows the transfer function for the voltage input mode.

$$V_{\text{OUT-V}} = V_{\text{D}} \times G + V_{\text{REF}} = -\left[ V_{\text{IN}} \times \frac{R_2}{R_1 + R_2} \right] \times G + V_{\text{REF}} \quad (4)$$

where

- $V_{\text{IN}}$  is the input voltage.

$R_1$  sets the input impedance of the voltage input mode. The minimum typical input impedance is 100 k $\Omega$ . The  $R_1$  value is 100 k $\Omega$  because increasing the  $R_1$  value also increases noise. The value of  $R_3$  must be extremely small compared to  $R_1$  and  $R_2$ . 20  $\Omega$  for  $R_3$  is selected because that resistance value is much smaller than  $R_1$  and yields an input voltage of  $\pm 400$  mV when operated in current mode ( $\pm 20$  mA).

Use Equation 5 to calculate  $R_2$  given  $V_D = \pm 400$  mV,  $V_{IN} = \pm 10$  V, and  $R_1 = 100$  k $\Omega$ .

$$V_D = V_{IN} \times \frac{R_2}{R_1 + R_2} \rightarrow R_2 = \frac{R_1 \times V_D}{V_{IN} - V_D} = 4.167 \text{ k}\Omega \quad (5)$$

The value obtained from Equation 5 is not a standard 0.1% value, so 4.17 k $\Omega$  is selected.  $R_1$  and  $R_2$  also use 0.1% tolerance resistors to minimize error.

Use Equation 6 to calculate the ideal gain of the instrumentation amplifier.

$$G = \frac{V_{OUT} - V_{REF}}{V_D} = \frac{4.8 \text{ V} - 2.5 \text{ V}}{400 \text{ mV}} = 5.75 \frac{\text{V}}{\text{V}} \quad (6)$$

Equation 7 calculates the gain-setting resistor value using the INA819 gain equation (Equation 1).

$$R_G = \frac{50 \text{ k}\Omega}{G - 1} = \frac{50 \text{ k}\Omega}{5.75 - 1} = 10.5 \text{ k}\Omega \quad (7)$$

Use a standard 0.1% resistor value of 10.5 k $\Omega$  for this design.

### 9.2.1.3 Application Curves

Figure 9-6 and Figure 9-7 show typical characteristic curves for the circuit in Figure 9-5.

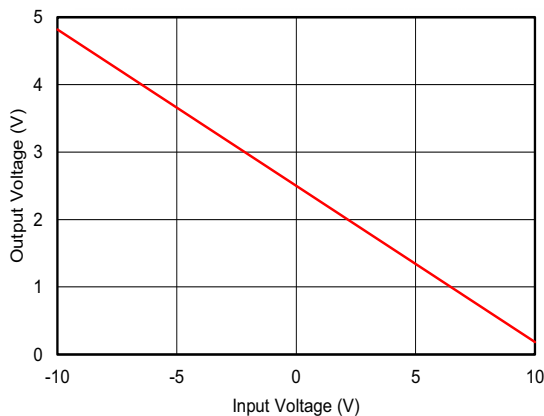


Figure 9-6. PLC Output Voltage vs Input Voltage

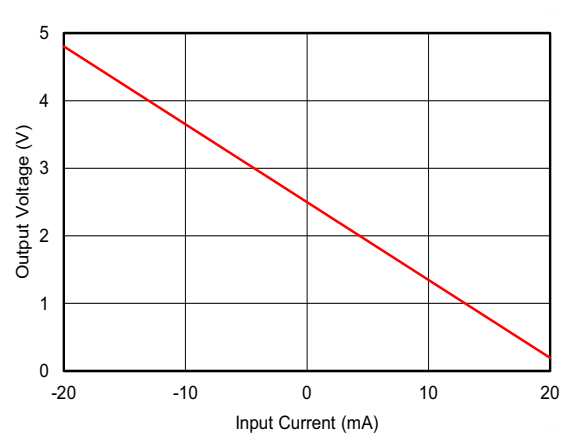
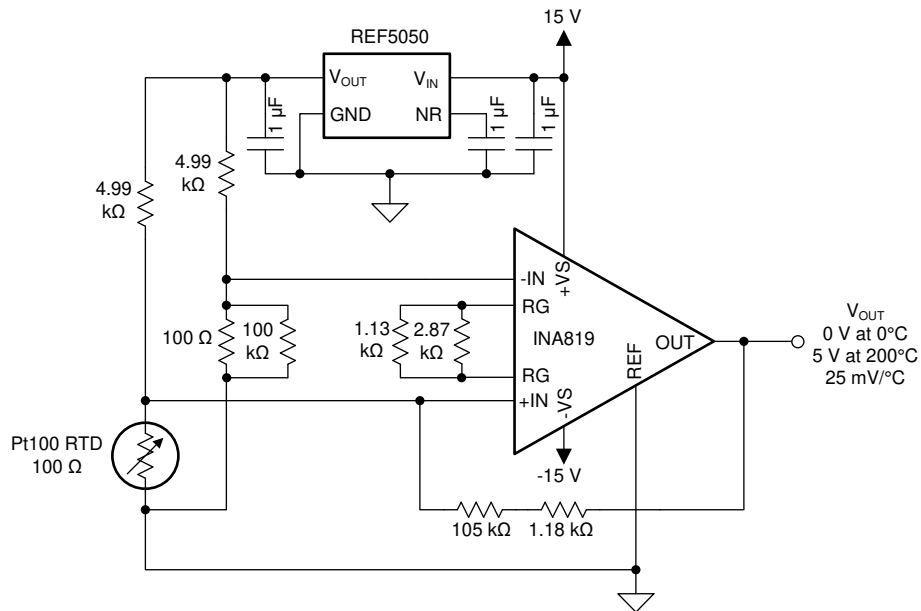


Figure 9-7. PLC Output Voltage vs Input Current

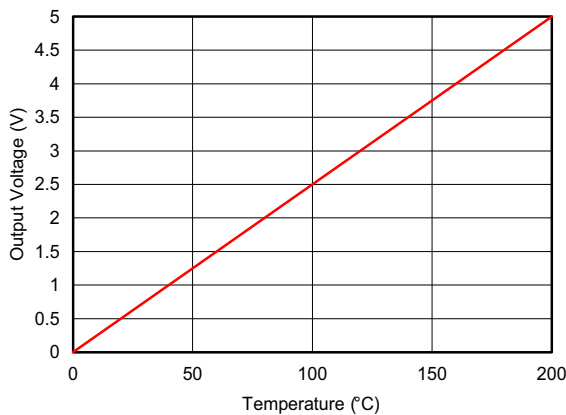
### 9.2.2 Resistance Temperature Detector Interface

Figure 9-8 illustrates a 3-wire interface circuit for resistance temperature detectors (RTDs). The circuit incorporates analog linearization and has an output voltage range from 0 V to 5 V. The linearization technique employed is described in *Analog linearization of resistance temperature detectors analog application journal*. Series and parallel combinations of standard 1% resistor values are used to achieve less than 0.02°C of error over a 200°C temperature span.

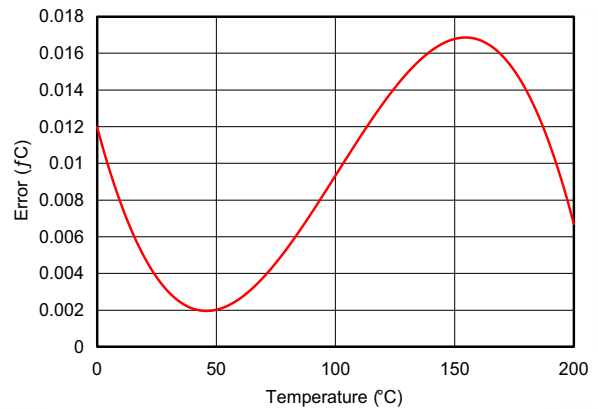


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**Figure 9-8. A 3-Wire Interface for RTDs With Analog Linearization**



**Figure 9-9. Transfer Function of a 3-Wire RTD Interface**



**Figure 9-10. Temperature Error Over the Full Temperature Range**

## 10 Power Supply Recommendations

The nominal performance of the INA819 is specified with a supply voltage of  $\pm 15$  V and midsupply reference voltage. The device also operates using power supplies from  $\pm 2.25$  V (4.5 V) to  $\pm 18$  V (36 V) and non-midsupply reference voltages with excellent performance. Parameters that can vary significantly with operating voltage and reference voltage are shown in the [Section 7.6](#) section.

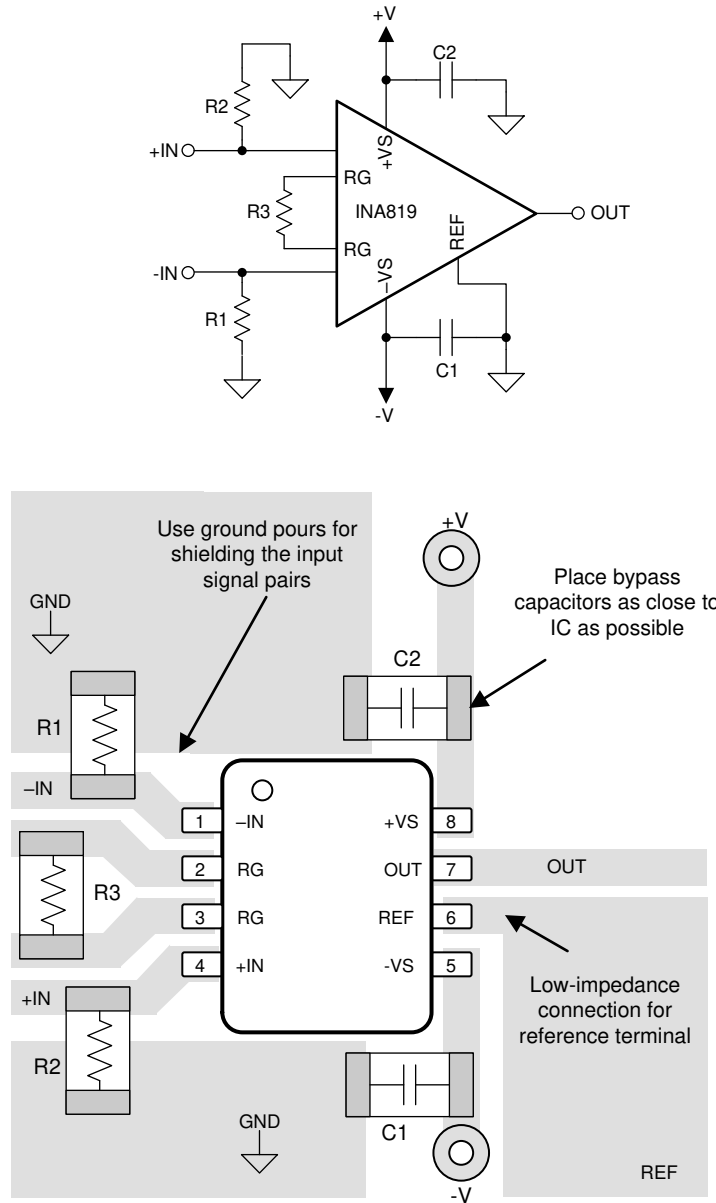
## 11 Layout

### 11.1 Layout Guidelines

Attention to good layout practices is always recommended. For best operational performance of the device, use good PCB layout practices, including:

- Take care to make sure that both input paths are well-matched for source impedance and capacitance to avoid converting common-mode signals into differential signals. Even slight mismatch in parasitic capacitance at the gain setting pins can degrade CMRR over frequency. For example, in applications that implement gain switching using switches or PhotoMOS<sup>®</sup> relays to change the value of  $R_G$ , select the component so that the switch capacitance is as small as possible and most importantly so that capacitance mismatch between the  $R_G$  pins is minimized.
- Noise can propagate into analog circuitry through the power pins of the circuit as a whole and of the device. Bypass capacitors reduce the coupled noise by providing low-impedance power sources local to the analog circuitry.
  - Connect low-ESR, 0.1- $\mu$ F ceramic bypass capacitors between each supply pin and ground, placed as close to the device as possible. A single bypass capacitor from  $V+$  to ground is applicable for single-supply applications.
- To reduce parasitic coupling, run the input traces as far away from the supply or output traces as possible. If these traces cannot be kept separate, crossing the sensitive trace perpendicular is much better than in parallel with the noisy trace.
- Place the external components as close to the device as possible. As shown in [Figure 11-1](#), keep  $R_G$  close to the pins to minimize parasitic capacitance.
- Keep the traces as short as possible.
- Connect exposed thermal pad to negative supply  $-V$ .

## 11.2 Layout Example



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**Figure 11-1. Example Schematic and Associated PCB Layout**

## 12 Device and Documentation Support

### 12.1 Device Support

#### 12.1.1 Development Support

##### 12.1.1.1 PSpice® for TI

PSpice® for TI is a design and simulation environment that helps evaluate performance of analog circuits. Create subsystem designs and prototype solutions before committing to layout and fabrication, reducing development cost and time to market.

##### 12.1.1.2 TINA-TI™ Simulation Software (Free Download)

TINA-TI™ simulation software is a simple, powerful, and easy-to-use circuit simulation program based on a SPICE engine. TINA-TI simulation software is a free, fully-functional version of the TINA™ software, preloaded with a library of macromodels, in addition to a range of both passive and active models. TINA-TI simulation software provides all the conventional dc, transient, and frequency domain analysis of SPICE, as well as additional design capabilities.

Available as a [free download](#) from the Analog eLab Design Center, TINA-TI simulation software offers extensive post-processing capability that allows users to format results in a variety of ways. Virtual instruments offer the ability to select input waveforms and probe circuit nodes, voltages, and waveforms, creating a dynamic quick-start tool.

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#### Note

These files require that either the TINA software or TINA-TI software be installed. Download the free TINA-TI simulation software from the [TINA-TI™ software folder](#).

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### 12.2 Documentation Support

#### 12.2.1 Related Documentation

For related documentation see the following:

Texas Instruments, [Comprehensive Error Calculation for Instrumentation Amplifiers application note](#)

#### 12.3 Receiving Notification of Documentation Updates

To receive notification of documentation updates, navigate to the device product folder on [ti.com](#). Click on *Subscribe to updates* to register and receive a weekly digest of any product information that has changed. For change details, review the revision history included in any revised document.

#### 12.4 Support Resources

TI E2E™ [support forums](#) are an engineer's go-to source for fast, verified answers and design help — straight from the experts. Search existing answers or ask your own question to get the quick design help you need.

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## 12.6 Electrostatic Discharge Caution



This integrated circuit can be damaged by ESD. Texas Instruments recommends that all integrated circuits be handled with appropriate precautions. Failure to observe proper handling and installation procedures can cause damage.

ESD damage can range from subtle performance degradation to complete device failure. Precision integrated circuits may be more susceptible to damage because very small parametric changes could cause the device not to meet its published specifications.

## 12.7 Glossary

[TI Glossary](#) This glossary lists and explains terms, acronyms, and definitions.

## 13 Mechanical, Packaging, and Orderable Information

The following pages include mechanical, packaging, and orderable information. This information is the most current data available for the designated devices. This data is subject to change without notice and revision of this document. For browser-based versions of this data sheet, refer to the left-hand navigation.

**PACKAGING INFORMATION**

Orderable part number	Status (1)	Material type (2)	Package   Pins	Package qty   Carrier	RoHS (3)	Lead finish/ Ball material (4)	MSL rating/ Peak reflow (5)	Op temp (°C)	Part marking (6)
<a href="#">INA819ID</a>	Active	Production	SOIC (D)   8	75   TUBE	Yes	NIPDAU	Level-2-260C-1 YEAR	-40 to 125	INA819
INA819ID.B	Active	Production	SOIC (D)   8	75   TUBE	Yes	NIPDAU	Level-2-260C-1 YEAR	-40 to 125	INA819
<a href="#">INA819IDGKR</a>	Active	Production	VSSOP (DGK)   8	2500   LARGE T&R	Yes	NIPDAU   SN   NIPDAUAG	Level-2-260C-1 YEAR	-40 to 125	1X3Q
INA819IDGKR.B	Active	Production	VSSOP (DGK)   8	2500   LARGE T&R	Yes	NIPDAU	Level-2-260C-1 YEAR	-40 to 125	1X3Q
<a href="#">INA819IDGKT</a>	Active	Production	VSSOP (DGK)   8	250   SMALL T&R	Yes	NIPDAU   SN   NIPDAUAG	Level-2-260C-1 YEAR	-40 to 125	1X3Q
INA819IDGKT.B	Active	Production	VSSOP (DGK)   8	250   SMALL T&R	Yes	NIPDAU	Level-2-260C-1 YEAR	-40 to 125	1X3Q
<a href="#">INA819IDR</a>	Active	Production	SOIC (D)   8	2500   LARGE T&R	Yes	NIPDAU	Level-2-260C-1 YEAR	-40 to 125	INA819
INA819IDR.B	Active	Production	SOIC (D)   8	2500   LARGE T&R	Yes	NIPDAU	Level-2-260C-1 YEAR	-40 to 125	INA819
<a href="#">INA819IDRGR</a>	Active	Production	SON (DRG)   8	3000   LARGE T&R	Yes	NIPDAU	Level-1-260C-UNLIM	-40 to 125	INA819
INA819IDRGR.B	Active	Production	SON (DRG)   8	3000   LARGE T&R	Yes	NIPDAU	Level-1-260C-UNLIM	-40 to 125	INA819
<a href="#">INA819IDRGT</a>	Active	Production	SON (DRG)   8	250   SMALL T&R	Yes	POST PLATE AG RING	Level-1-260C-UNLIM	-40 to 125	INA819
INA819IDRGT.B	Active	Production	SON (DRG)   8	250   SMALL T&R	Yes	POST PLATE AG RING	Level-1-260C-UNLIM	-40 to 125	INA819
INA819IDRGTG4	Active	Production	SON (DRG)   8	250   SMALL T&R	Yes	NIPDAU	Level-1-260C-UNLIM	-40 to 125	INA819
INA819IDRGTG4.B	Active	Production	SON (DRG)   8	250   SMALL T&R	Yes	NIPDAU	Level-1-260C-UNLIM	-40 to 125	INA819

(1) **Status:** For more details on status, see our [product life cycle](#).

(2) **Material type:** When designated, preproduction parts are prototypes/experimental devices, and are not yet approved or released for full production. Testing and final process, including without limitation quality assurance, reliability performance testing, and/or process qualification, may not yet be complete, and this item is subject to further changes or possible discontinuation. If available for ordering, purchases will be subject to an additional waiver at checkout, and are intended for early internal evaluation purposes only. These items are sold without warranties of any kind.

(3) **RoHS values:** Yes, No, RoHS Exempt. See the [TI RoHS Statement](#) for additional information and value definition.

(4) **Lead finish/Ball material:** Parts may have multiple material finish options. Finish options are separated by a vertical ruled line. Lead finish/Ball material values may wrap to two lines if the finish value exceeds the maximum column width.

(5) **MSL rating/Peak reflow:** The moisture sensitivity level ratings and peak solder (reflow) temperatures. In the event that a part has multiple moisture sensitivity ratings, only the lowest level per JEDEC standards is shown. Refer to the shipping label for the actual reflow temperature that will be used to mount the part to the printed circuit board.

**(6) Part marking:** There may be an additional marking, which relates to the logo, the lot trace code information, or the environmental category of the part.

Multiple part markings will be inside parentheses. Only one part marking contained in parentheses and separated by a "~" will appear on a part. If a line is indented then it is a continuation of the previous line and the two combined represent the entire part marking for that device.

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**TAPE AND REEL INFORMATION**

**QUADRANT ASSIGNMENTS FOR PIN 1 ORIENTATION IN TAPE**


\*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Reel Diameter (mm)	Reel Width W1 (mm)	A0 (mm)	B0 (mm)	K0 (mm)	P1 (mm)	W (mm)	Pin1 Quadrant
INA819IDGKR	VSSOP	DGK	8	2500	330.0	12.4	5.25	3.35	1.25	8.0	12.0	Q1
INA819IDGKR	VSSOP	DGK	8	2500	330.0	12.4	5.3	3.4	1.4	8.0	12.0	Q1
INA819IDGKR	VSSOP	DGK	8	2500	330.0	12.4	5.3	3.4	1.4	8.0	12.0	Q1
INA819IDGKT	VSSOP	DGK	8	250	330.0	12.4	5.25	3.35	1.25	8.0	12.0	Q1
INA819IDGKT	VSSOP	DGK	8	250	330.0	12.4	5.3	3.4	1.4	8.0	12.0	Q1
INA819IDR	SOIC	D	8	2500	330.0	12.4	6.4	5.2	2.1	8.0	12.0	Q1
INA819IDRGR	SON	DRG	8	3000	330.0	12.4	3.3	3.3	1.1	8.0	12.0	Q2
INA819IDRGT	SON	DRG	8	250	180.0	12.4	3.3	3.3	1.1	8.0	12.0	Q2
INA819IDRGTG4	SON	DRG	8	250	180.0	12.4	3.3	3.3	1.1	8.0	12.0	Q2

**TAPE AND REEL BOX DIMENSIONS**


\*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Length (mm)	Width (mm)	Height (mm)
INA819IDGKR	VSSOP	DGK	8	2500	366.0	364.0	50.0
INA819IDGKR	VSSOP	DGK	8	2500	353.0	353.0	32.0
INA819IDGKR	VSSOP	DGK	8	2500	366.0	364.0	50.0
INA819IDGKT	VSSOP	DGK	8	250	366.0	364.0	50.0
INA819IDGKT	VSSOP	DGK	8	250	353.0	353.0	32.0
INA819IDR	SOIC	D	8	2500	353.0	353.0	32.0
INA819IDRGR	SON	DRG	8	3000	367.0	367.0	35.0
INA819IDRGT	SON	DRG	8	250	210.0	185.0	35.0
INA819IDRGTG4	SON	DRG	8	250	210.0	185.0	35.0

**TUBE**


\*All dimensions are nominal

Device	Package Name	Package Type	Pins	SPQ	L (mm)	W (mm)	T (μm)	B (mm)
INA819ID	D	SOIC	8	75	506.6	8	3940	4.32
INA819ID.B	D	SOIC	8	75	506.6	8	3940	4.32

# DGK0008A



# PACKAGE OUTLINE

VSSOP - 1.1 mm max height

SMALL OUTLINE PACKAGE



4214862/A 04/2023

**NOTES:**

PowerPAD is a trademark of Texas Instruments.

1. All linear dimensions are in millimeters. Any dimensions in parenthesis are for reference only. Dimensioning and tolerancing per ASME Y14.5M.
2. This drawing is subject to change without notice.
3. This dimension does not include mold flash, protrusions, or gate burrs. Mold flash, protrusions, or gate burrs shall not exceed 0.15 mm per side.
4. This dimension does not include interlead flash. Interlead flash shall not exceed 0.25 mm per side.
5. Reference JEDEC registration MO-187.

# EXAMPLE BOARD LAYOUT

DGK0008A

™ VSSOP - 1.1 mm max height

SMALL OUTLINE PACKAGE



LAND PATTERN EXAMPLE  
EXPOSED METAL SHOWN  
SCALE: 15X



SOLDER MASK DETAILS

4214862/A 04/2023

NOTES: (continued)

6. Publication IPC-7351 may have alternate designs.
7. Solder mask tolerances between and around signal pads can vary based on board fabrication site.
8. Vias are optional depending on application, refer to device data sheet. If any vias are implemented, refer to their locations shown on this view. It is recommended that vias under paste be filled, plugged or tented.
9. Size of metal pad may vary due to creepage requirement.

# EXAMPLE STENCIL DESIGN

DGK0008A

™ VSSOP - 1.1 mm max height

SMALL OUTLINE PACKAGE



SOLDER PASTE EXAMPLE  
SCALE: 15X

4214862/A 04/2023

NOTES: (continued)

11. Laser cutting apertures with trapezoidal walls and rounded corners may offer better paste release. IPC-7525 may have alternate design recommendations.
12. Board assembly site may have different recommendations for stencil design.

## GENERIC PACKAGE VIEW

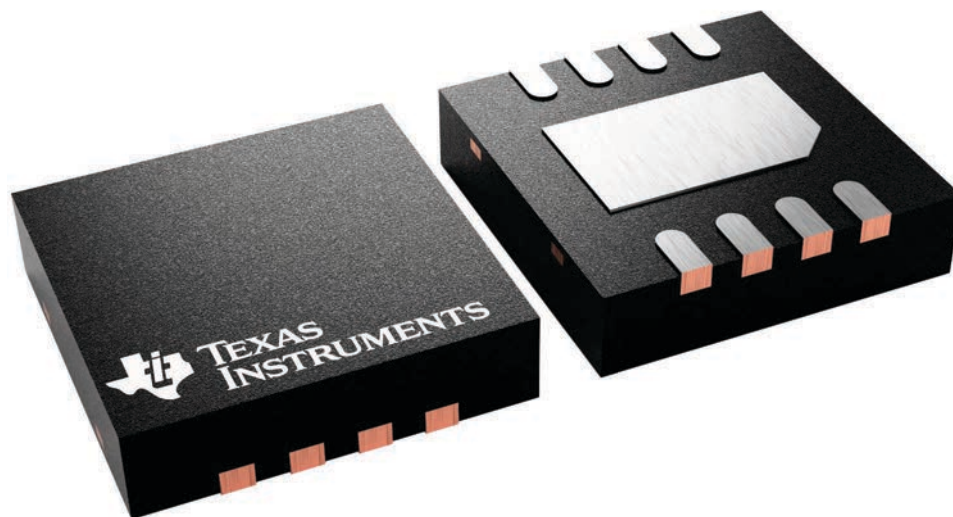
**DRG 8**

**WSO - 0.8 mm max height**

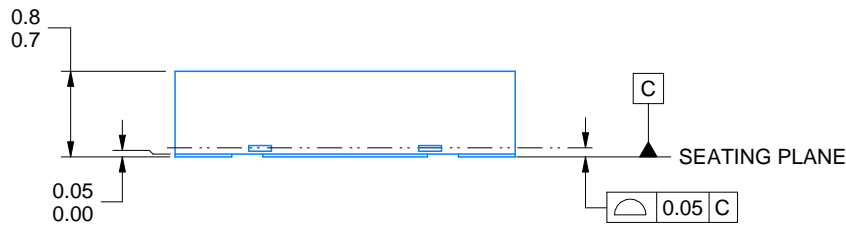
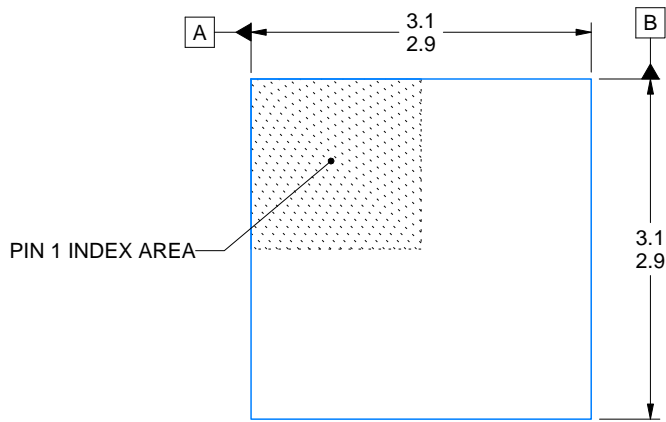
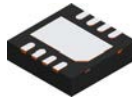
3 x 3, 0.5 mm pitch

PLASTIC SMALL OUTLINE - NO LEAD

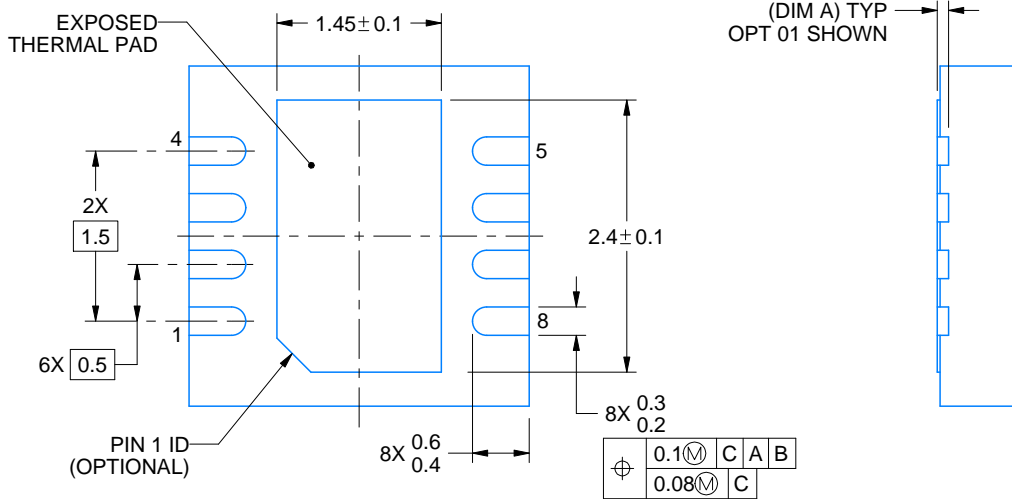
This image is a representation of the package family, actual package may vary.  
Refer to the product data sheet for package details.



4225794/A



DIMENSION A	
OPTION 01	(0.1)
OPTION 02	(0.2)



4218886/A 01/2020

NOTES:

1. All linear dimensions are in millimeters. Any dimensions in parenthesis are for reference only. Dimensioning and tolerancing per ASME Y14.5M.
2. This drawing is subject to change without notice.
3. The package thermal pad must be soldered to the printed circuit board for thermal and mechanical performance.

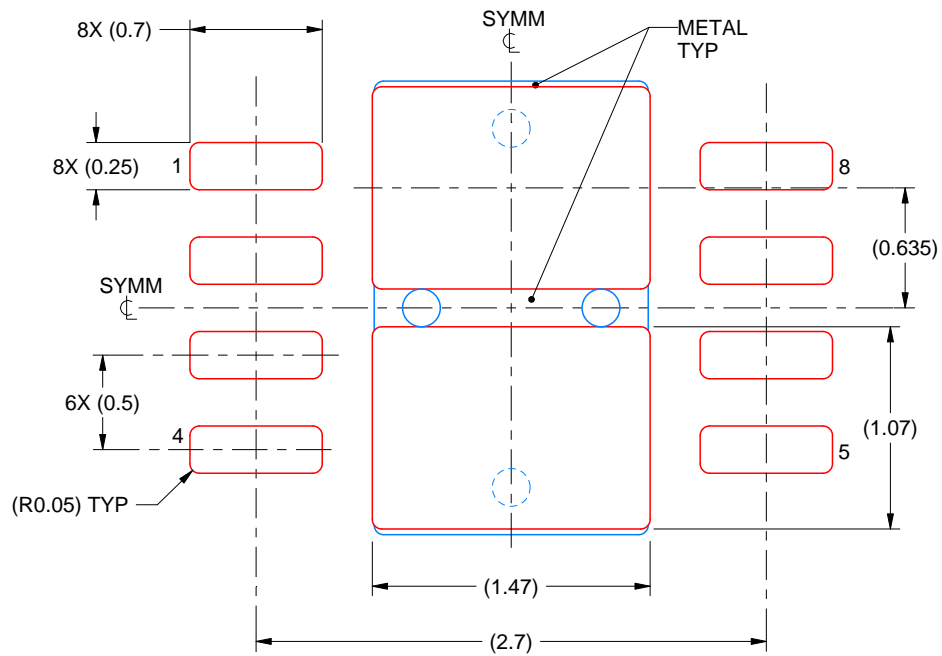


# EXAMPLE STENCIL DESIGN

DRG0008B

WSO - 0.8 mm max height

PLASTIC SMALL OUTLINE - NO LEAD



SOLDER PASTE EXAMPLE  
BASED ON 0.125 mm THICK STENCIL

EXPOSED PAD  
82% PRINTED SOLDER COVERAGE BY AREA  
SCALE:25X

4218886/A 01/2020

NOTES: (continued)

6. Laser cutting apertures with trapezoidal walls and rounded corners may offer better paste release. IPC-7525 may have alternate design recommendations.



D0008A

# PACKAGE OUTLINE

SOIC - 1.75 mm max height

SMALL OUTLINE INTEGRATED CIRCUIT



4214825/C 02/2019

### NOTES:

1. Linear dimensions are in inches [millimeters]. Dimensions in parenthesis are for reference only. Controlling dimensions are in inches. Dimensioning and tolerancing per ASME Y14.5M.
2. This drawing is subject to change without notice.
3. This dimension does not include mold flash, protrusions, or gate burrs. Mold flash, protrusions, or gate burrs shall not exceed  $.006$  [0.15] per side.
4. This dimension does not include interlead flash.
5. Reference JEDEC registration MS-012, variation AA.

# EXAMPLE BOARD LAYOUT

D0008A

SOIC - 1.75 mm max height

SMALL OUTLINE INTEGRATED CIRCUIT



LAND PATTERN EXAMPLE  
 EXPOSED METAL SHOWN  
 SCALE:8X



SOLDER MASK DETAILS

4214825/C 02/2019

NOTES: (continued)

- 6. Publication IPC-7351 may have alternate designs.
- 7. Solder mask tolerances between and around signal pads can vary based on board fabrication site.

# EXAMPLE STENCIL DESIGN

D0008A

SOIC - 1.75 mm max height

SMALL OUTLINE INTEGRATED CIRCUIT



SOLDER PASTE EXAMPLE  
BASED ON .005 INCH [0.125 MM] THICK STENCIL  
SCALE:8X

4214825/C 02/2019

NOTES: (continued)

8. Laser cutting apertures with trapezoidal walls and rounded corners may offer better paste release. IPC-7525 may have alternate design recommendations.
9. Board assembly site may have different recommendations for stencil design.

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