**DESCRIPTION**

The INA326 and INA327 (with shutdown) are high-performance, low-cost, precision instrumentation amplifiers with rail-to-rail input and output. They are true single-supply instrumentation amplifiers with very low DC errors and input common-mode ranges that extends beyond the positive and negative rails. These features make them suitable for applications ranging from general-purpose to high-accuracy.

Excellent long-term stability and very low 1/f noise assure low offset voltage and drift throughout the life of the product.

The INA326 (without shutdown) comes in the MSOP-8 package. The INA327 (with shutdown) is offered in an MSOP-10. Both are specified over the industrial temperature range, –40°C to +85°C, with operation from –40°C to +125°C.

**APPLICATIONS**

- **LOW-LEVEL TRANSDUCER AMPLIFIER FOR BRIDGES, LOAD CELLS, THERMOCOUPLES**
- **WIDE DYNAMIC RANGE SENSOR MEASUREMENTS**
- **HIGH-RESOLUTION TEST SYSTEMS**
- **WEIGH SCALES**
- **MULTI-CHANNEL DATA ACQUISITION SYSTEMS**
- **MEDICAL INSTRUMENTATION**
- **GENERAL-PURPOSE**
**PACKAGE/ORDERING INFORMATION**

<table>
<thead>
<tr>
<th>PRODUCT</th>
<th>PACKAGE-LEAD</th>
<th>PACKAGE DESIGNATOR</th>
<th>SPECIFIED TEMPERATURE RANGE</th>
<th>PACKAGE MARKING</th>
<th>ORDERING NUMBER</th>
<th>TRANSPORT MEDIA, QUANTITY</th>
</tr>
</thead>
<tbody>
<tr>
<td>INA326</td>
<td>MSOP-8</td>
<td>DGK</td>
<td>–40°C to +85°C</td>
<td>B26</td>
<td>INA326EA/250</td>
<td>Tape and Reel, 250</td>
</tr>
<tr>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td>INA326EA/2K5</td>
<td>Tape and Reel, 2500</td>
</tr>
<tr>
<td>INA327</td>
<td>MSOP-10</td>
<td>DGS</td>
<td>–40°C to +85°C</td>
<td>B27</td>
<td>INA327EA/250</td>
<td>Tape and Reel, 250</td>
</tr>
<tr>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td>INA327EA/2K5</td>
<td>Tape and Reel, 2500</td>
</tr>
</tbody>
</table>

**ABSOLUTE MAXIMUM RATINGS**

Supply Voltage: +5.5V

Signal Input Terminals: Voltage: –0.5V to (V+) + 0.5V, Current: ±10mA

Output Short-Circuit: Continuous

Operating Temperature Range: –40°C to +125°C

Storage Temperature Range: –65°C to +150°C

Junction Temperature: +150°C

Lead Temperature (soldering, 10s): +300°C

NOTES: (1) Stresses above these ratings may cause permanent damage. Exposure to absolute maximum conditions for extended periods may degrade device reliability. These are stress ratings only, and functional operation of the device at these or any other conditions beyond those specified is not implied.

(2) Input terminals are diode clamped to the power-supply rails. Input signals that can swing more than 0.5V beyond the supply rails should be current limited to 10mA or less.

**ELECTROSTATIC DISCHARGE SENSITIVITY**

This integrated circuit can be damaged by ESD. Texas Instruments recommends that all integrated circuits be handled with appropriate precautions. Failure to observe proper handling and installation procedures can cause damage.

ESD damage can range from subtle performance degradation to complete device failure. Precision integrated circuits may be more susceptible to damage because very small parametric changes could cause the device not to meet its published specifications.

**PIN CONFIGURATION**

![INA326 Pin Configuration](image)

![INA327 Pin Configuration](image)
ELECTRICAL CHARACTERISTICS: $V_S = +2.7\, \text{V} \, \text{to} \, +5.5\, \text{V}$

**BOLDFACE** limits apply over the specified temperature range, $T_A = -40^\circ\text{C} \, \text{to} \, +85^\circ\text{C}$

At $T_A = +25^\circ\text{C}$, $R_L = 10\, \text{k}\Omega$, $G = 100$ ($R_1 = 2\, \text{k}\Omega$, $R_2 = 100\, \text{k}\Omega$), external gain set resistors, and $I_{\text{COMMON}} = V_S/2$, with external equivalent filter corner of 1kHz, unless otherwise noted.

<table>
<thead>
<tr>
<th>PARAMETER</th>
<th>CONDITION</th>
<th>MIN</th>
<th>TYP</th>
<th>MAX</th>
<th>UNITS</th>
</tr>
</thead>
<tbody>
<tr>
<td><strong>INPUT</strong></td>
<td>$V_{OS}$</td>
<td>$V_S = +5, \text{V}$, $V_{CM} = V_S/2$</td>
<td>±20</td>
<td>±100</td>
<td>µV</td>
</tr>
<tr>
<td><strong>Offset Voltage, RTI</strong></td>
<td>$V_{OS}$</td>
<td>$V_S = +5, \text{V}$, $V_{CM} = V_S/2$</td>
<td>±0.1</td>
<td>±124</td>
<td>µV</td>
</tr>
<tr>
<td><strong>Over Temperature</strong></td>
<td>$dV_{OS}/dT$</td>
<td>$V_S = +2.7, \text{V} , \text{to} , +5.5, \text{V}$, $V_{CM} = V_S/2$</td>
<td>±3</td>
<td>±0.4</td>
<td>µV/°C</td>
</tr>
<tr>
<td><strong>Noise Voltage, RTI</strong></td>
<td>$V_{CM} = V_S/2$</td>
<td>$V_S = +5, \text{V}$, $V_{CM} = V_S/2$</td>
<td>±0.2</td>
<td>±2</td>
<td>nA</td>
</tr>
<tr>
<td><strong>Possible Bias Current</strong></td>
<td>$I_B$</td>
<td>$V_S = +5, \text{V}$</td>
<td>See Typical Characteristics</td>
<td></td>
<td></td>
</tr>
<tr>
<td><strong>Noise Current, RTI</strong></td>
<td>$I_{OS}$</td>
<td>$V_S = +5, \text{V}$</td>
<td>±0.2</td>
<td>±2</td>
<td>nA</td>
</tr>
<tr>
<td><strong>Gain Equation</strong></td>
<td>$G = 2(R_2/R_1)$</td>
<td>$G = 10$, $100$, $V_S = +5, \text{V}$, $V_O = 0.075, \text{V}$ to $4.925, \text{V}$</td>
<td>±0.08</td>
<td>±0.2</td>
<td>ppm/°C</td>
</tr>
<tr>
<td><strong>Gain Error</strong></td>
<td>$G = 10$, $100$, $V_S = +5, \text{V}$, $V_O = 0.075, \text{V}$ to $4.925, \text{V}$</td>
<td>±6</td>
<td>±25</td>
<td>ppm/°C</td>
<td></td>
</tr>
<tr>
<td><strong>Output Voltage Swing from Rail</strong></td>
<td>$R_L = 100, \text{k}\Omega$</td>
<td>$V_S = +5, \text{V}$</td>
<td>5</td>
<td>mV</td>
<td></td>
</tr>
<tr>
<td><strong>Over Temperature</strong></td>
<td>$R_L = 10, \text{k}\Omega$, $V_S = +5, \text{V}$</td>
<td>75</td>
<td>10</td>
<td>mV</td>
<td></td>
</tr>
<tr>
<td><strong>Capacitive Load Drive</strong></td>
<td>$I_{\text{LAC}}$</td>
<td>±25</td>
<td>mA</td>
<td></td>
<td></td>
</tr>
<tr>
<td><strong>INTERNAL OSCILLATOR</strong></td>
<td>Frequency of Auto-Correction</td>
<td>90</td>
<td>kHz</td>
<td></td>
<td></td>
</tr>
<tr>
<td><strong>Accuracy</strong></td>
<td>±20</td>
<td>%</td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td><strong>FREQUENCY RESPONSE</strong></td>
<td>Bandwidth(4), –3dB</td>
<td>$G = 1$ to $1, \text{k}$</td>
<td>1</td>
<td>kHz</td>
<td></td>
</tr>
<tr>
<td><strong>Slew Rate(4)</strong></td>
<td>$V_S = +5, \text{V}$, All Gains, $C_L = 100, \text{pF}$</td>
<td>$1, \text{k}\Omega$ Filter, $G = 1$ to $1, \text{k}$, $V_O = 2, \text{V}$ step, $C_L = 100, \text{pF}$</td>
<td>0.95</td>
<td>ms</td>
<td></td>
</tr>
<tr>
<td><strong>Settling Time</strong></td>
<td>$t_{\text{sg}}$</td>
<td>$10, \text{kHz}$ Filter, $G = 1$ to $1, \text{k}$, $V_O = 2, \text{V}$ step, $C_L = 100, \text{pF}$</td>
<td>1.3</td>
<td>ms</td>
<td></td>
</tr>
<tr>
<td><strong>Overload Recovery</strong></td>
<td>$t_{\text{ov}}$</td>
<td>$1, \text{k}\Omega$ Filter, 50% Output Overload, $G = 1$ to $1, \text{k}$</td>
<td>30</td>
<td>µs</td>
<td></td>
</tr>
</tbody>
</table>

**INA326, INA327**

SBOS222D

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### ELECTRICAL CHARACTERISTICS: $V_S = +2.7V$ to $+5.5V$ (Cont.)

**BOLDFACE** limits apply over the specified temperature range, $T_A = -40^\circ C$ to $+85^\circ C$

At $T_A = +25^\circ C$, $R_L = 10k\Omega$, $G = 100$ ($R_1 = 2k\Omega$, $R_2 = 100k\Omega$), external gain set resistors, and $I_{A\text{COMMON}} = V_S/2$, with external equivalent filter corner of 1kHz, unless otherwise noted.

<table>
<thead>
<tr>
<th>PARAMETER</th>
<th>CONDITION</th>
<th>INA326EA, INA327EA</th>
</tr>
</thead>
<tbody>
<tr>
<td></td>
<td></td>
<td><strong>MIN</strong></td>
</tr>
<tr>
<td><strong>POWER SUPPLY</strong></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Specified Voltage Range</td>
<td>$+2.7$</td>
<td>$+5.5$</td>
</tr>
<tr>
<td>Quiescent Current</td>
<td>$I_Q$</td>
<td>$I_Q = 0$, Diff $V_{IN} = 0V$, $V_S = +5V$</td>
</tr>
<tr>
<td>Over Temperature</td>
<td>$I_Q$</td>
<td>$I_Q = 0$, Diff $V_{IN} = 0V$, $V_S = +5V$</td>
</tr>
<tr>
<td><strong>SHUTDOWN</strong></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Disable (Logic Low Threshold)</td>
<td>$1.6$</td>
<td>$0.25$</td>
</tr>
<tr>
<td>Enable (Logic High Threshold)</td>
<td>$1.6$</td>
<td>$0.25$</td>
</tr>
<tr>
<td>Enable Time$^{(5)}$</td>
<td>$75$</td>
<td>$\mu$s</td>
</tr>
<tr>
<td>Disable Time</td>
<td>$100$</td>
<td>$\mu$s</td>
</tr>
<tr>
<td>Shutdown Current and Enable Pin Current</td>
<td>$V_S = +5V$, Disabled</td>
<td>$150$</td>
</tr>
<tr>
<td><strong>TEMPERATURE RANGE</strong></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Specified Range</td>
<td>$-40$</td>
<td>$+85$</td>
</tr>
<tr>
<td>Operating Range</td>
<td>$-40$</td>
<td>$+125$</td>
</tr>
<tr>
<td>Storage Range</td>
<td>$-65$</td>
<td>$+150$</td>
</tr>
<tr>
<td>Thermal Resistance</td>
<td>$\theta_{JA}$</td>
<td>MSOP-8, MSOP-10 Surface-Mount</td>
</tr>
</tbody>
</table>

**NOTES:**
1. 1000-hour life test at $150^\circ C$ demonstrated randomly distributed variation in the range of measurement limits—approximately $10\mu V$.
2. See Applications Information section, and Figures 1 and 3.
3. Does not include error and TCR of external gain-setting resistors.
4. Dynamic response is limited by filtering. Higher bandwidths can be achieved by adjusting the filter.
5. See Typical Characteristics, “Input Offset Voltage vs Warm-Up Time”.

---

**PARAMETER CONDITION**

**MIN** | **TYP** | **MAX** | **UNITS**

**POWER SUPPLY**

Specified Voltage Range | $+2.7$ | $+5.5$ | $2.4$ | $3.4$ | $3.7$ | mA

Quiescent Current | $I_Q$ | $I_Q = 0$, Diff $V_{IN} = 0V$, $V_S = +5V$ | $+2.7$ | $2.4$ | $3.4$ | $3.7$ | mA

Over Temperature | $I_Q$ | $I_Q = 0$, Diff $V_{IN} = 0V$, $V_S = +5V$ | $+2.7$ | $2.4$ | $3.4$ | $3.7$ | mA

**SHUTDOWN**

Disable (Logic Low Threshold) | $1.6$ | $0.25$ | $75$ | $\mu$s | $100$ | $\mu$s | $2$ | $5$ | $\mu$A

Enable (Logic High Threshold) | $1.6$ | $0.25$ | $75$ | $\mu$s | $100$ | $\mu$s | $2$ | $5$ | $\mu$A

Enable Time$^{(5)}$ | $75$ | $\mu$s | $100$ | $\mu$s | $2$ | $5$ | $\mu$A

Disable Time | $100$ | $\mu$s | $2$ | $5$ | $\mu$A

Shutdown Current and Enable Pin Current | $V_S = +5V$, Disabled | $150$ | $\mu$A

**TEMPERATURE RANGE**

Specified Range | $-40$ | $+85$ | $-65$ | $+150$ | $\circ C$

Operating Range | $-40$ | $+125$ | $-65$ | $+150$ | $\circ C$

Storage Range | $-65$ | $+150$ | $-65$ | $+150$ | $\circ C$

Thermal Resistance | $\theta_{JA}$ | MSOP-8, MSOP-10 Surface-Mount | $150$ | $\circ C/W$
TYPICAL CHARACTERISTICS

At $T_A = 25^\circ C$, $V_S = \pm 5V$, Gain = 100, and $R_L = 10k\Omega$ with external equivalent filter corner of 1kHz, unless otherwise noted.
TYPICAL CHARACTERISTICS (Cont.)

At $T_A = 25^\circ C$, $V_s = +5V$, Gain = 100, and $R_L = 10k\Omega$ with external equivalent filter corner of 1kHz, unless otherwise noted.

**INPUT OFFSET VOLTAGE vs TURN-ON TIME**
1kHz FILTER, $G = 100$

**INPUT OFFSET VOLTAGE vs WARM-UP TIME**
10kHz FILTER, $G = 100$

**SMALL-SIGNAL RESPONSE**
$G = 1, 10, \text{ AND } 100$

**SMALL-SIGNAL STEP RESPONSE**
$G = 1000$

**LARGE-SIGNAL RESPONSE**
$G = 1 \text{ TO } 1000$

**0.01Hz TO 10Hz VOLTAGE NOISE**

---

**INPUT OFFSET VOLTAGE vs TURN-ON TIME**

**INPUT OFFSET VOLTAGE vs WARM-UP TIME**

**SMALL-SIGNAL RESPONSE**

**SMALL-SIGNAL STEP RESPONSE**

**LARGE-SIGNAL RESPONSE**

**0.01Hz TO 10Hz VOLTAGE NOISE**

---

**INPUT OFFSET VOLTAGE vs TURN-ON TIME**

**INPUT OFFSET VOLTAGE vs WARM-UP TIME**

**SMALL-SIGNAL RESPONSE**

**SMALL-SIGNAL STEP RESPONSE**

**LARGE-SIGNAL RESPONSE**

**0.01Hz TO 10Hz VOLTAGE NOISE**

---

**INPUT OFFSET VOLTAGE vs TURN-ON TIME**

**INPUT OFFSET VOLTAGE vs WARM-UP TIME**

**SMALL-SIGNAL RESPONSE**

**SMALL-SIGNAL STEP RESPONSE**

**LARGE-SIGNAL RESPONSE**

**0.01Hz TO 10Hz VOLTAGE NOISE**
TYPICAL CHARACTERISTICS (Cont.)

At $T_A = 25\, ^\circ\text{C}$, $V_S = +5\, \text{V}$, Gain = 100, and $R_L = 10\, \text{k}\Omega$ with external equivalent filter corner of 1kHz, unless otherwise noted.

OFFSET VOLTAGE DRIFT PRODUCTION DISTRIBUTION

G = 1

OFFSET VOLTAGE PRODUCTION DISTRIBUTION

G = 1

OFFSET VOLTAGE DRIFT PRODUCTION DISTRIBUTION

G = 10

OFFSET VOLTAGE PRODUCTION DISTRIBUTION

G = 10

OFFSET VOLTAGE DRIFT PRODUCTION DISTRIBUTION

G = 100, 1000

OFFSET VOLTAGE PRODUCTION DISTRIBUTION

G = 100, 1000
TYPICAL CHARACTERISTICS (Cont.)

At $T_A = 25^\circ C$, $V_S = +5V$, Gain = 100, and $R_L = 10k\Omega$ with external equivalent filter corner of 1kHz, unless otherwise noted.
APPLICATIONS INFORMATION

Figure 1 shows the basic connections required for operation of the INA326. A 0.1µF capacitor, placed close to and across the power-supply pins is strongly recommended for highest accuracy. R1C0 is an output filter that minimizes auto-correction circuitry noise. This output filter may also serve as an anti-aliasing filter ahead of an Analog-to-Digital (A/D) converter. It is also optional based on desired precision.

The output reference terminal is taken at the low side of R2 (IA COMMON).

The INA326 uses a unique internal topology to achieve excellent Common-Mode Rejection (CMR). Unlike conventional instrumentation amplifiers, CMR is not affected by resistance in the reference connections or sockets. See “Inside the INA326” for further detail. To achieve best high-frequency CMR, minimize capacitance on pins 1 and 8.

| DESIRED GAIN | R1 (Ω) | R2 || C2 (Ω || nF) |
|--------------|--------|---------------------|
| 0.1          | 400k   | 20k || 5         |
| 0.2          | 400k   | 40k || 2.5      |
| 0.5          | 400k   | 100k || 1       |
| 1            | 200k   | 100k || 1       |
| 2            | 100k   | 100k || 1       |
| 5            | 40k    | 100k || 1       |
| 10           | 20k    | 100k || 1       |
| 50           | 4k     | 100k || 1       |
| 100          | 2k     | 100k || 1       |
| 200          | 2k     | 200k || 0.5     |
| 500          | 2k     | 500k || 0.2     |
| 1000         | 2k     | 1M   || 0.1      |
| 2000         | 2k     | 2M   || 0.05     |
| 5000         | 2k     | 5M   || 0.02     |
| 10000        | 2k     | 10M  || 0.01     |

NOTES: (1) C2 and C0 combine to form a 2-pole response that is –3dB at 1kHz. Each individual pole is at 1.5kHz. (2) Output voltage is referenced to IA COMMON (see text). (3) Output offset voltage required for measurement near zero (see Figure 28).

SETTING THE GAIN

The INA326 is a 2-stage amplifier with each stage gain set by R1 and R2, respectively (see Figure 5, “Inside the INA326”, for details). Overall gain is described by the equation:

\[ G = \frac{2R_2}{R_1} \]

(1)

The stability and temperature drift of the external gain-setting resistors will affect gain by an amount that can be directly inferred from the gain equation (1).

Resistor values for commonly used gains are shown in Figure 1. Gain-set resistor values for best performance are different for +5V single-supply and for ±2.5V dual-supply operation. Optimum value for R1 can be calculated by:

\[ R_1 = \frac{V_{IN, MAX}}{12.5\mu A} \]

(2)

where R1 must be no less than 2kΩ.

NOTE: Connections for INA327 differ—see Pin Configuration for detail.
Following this design procedure for \( R_1 \) produces the maximum possible input stage gain for best accuracy and lowest noise. Circuit layout and supply bypassing can affect performance. Minimize the stray capacitance on pins 1 and 8. Use recommended supply bypassing, including a capacitor directly from pin 7 to pin 4 (V+ to V–), even with dual (split) power supplies (see Figure 1).

**OFFSET VOLTAGE, DRIFT, AND CIRCUIT VALUES**

As with other multi-stage instrumentation amplifiers, input-referred offset voltage depends on gain and circuit values. The specified offset and drift performance is rated at \( R_1 = 2k\Omega \), \( R_2 = 100k\Omega \), and \( V_S = \pm 2.5V \). Offset voltage and drift for other circuit values can be estimated from the following equations:

\[
V_{OS} = 10\mu V + (50nA)(R_2)/G \tag{3}
\]

\[
dV_{OS}/dT = 0.12\mu V/°C + (0.16nA/°C)(R_2)/G \tag{4}
\]

These equations might imply that offset and drift can be minimized by making the value of \( R_2 \) much lower than the values indicated in Figure 1. These values, however, have been chosen to assure that the output current into \( R_2 \) is kept less than or equal to \( \pm 25\mu A \), while maintaining \( R_1 \)'s value greater than or equal to 2k\Omega. Some applications with limited output voltage swing or low power-supply voltage may allow lower values for \( R_2 \), thus providing lower input-referred offset voltage and offset voltage drift.

Conversely, single-supply operation with \( R_2 \) grounded requires that \( R_2 \) values be made larger to assure that current remains under 25\muA. This will increase the input-referred offset voltage and offset voltage drift.

Circuit conditions that cause more than 25\muA to flow in \( R_2 \) will not cause damage, but may produce more nonlinearity.

**INA327 ENABLE FUNCTION**

The INA327 adds an enable/shutdown function to the INA326. Its pinout differs from the INA326—see the Pin Configuration for detail.

The INA327 can be enabled by applying a logic HIGH voltage level to the Enable pin. Conversely, a logic LOW voltage level will disable the amplifier, reducing its supply current from 2.4mA to typically 2\muA. For battery-operated applications, this feature may be used to greatly reduce the average current and extend battery life. This pin should be connected to a valid high or low voltage or driven, not left open circuit. The Enable pin can be modeled as a CMOS input gate as in Figure 2.

\[ V_+ \]

\[ \text{Enable} \]

\[ 2\mu A \]

**Figure 2. Enable Pin Model.**

The enable time following shutdown is 75\mu s plus the settling time due to filters (see Typical Characteristics, “Input Offset Voltage vs Warm-up Time”). Disable time is 100\mu s. This allows the INA327 to be operated as a “gated” amplifier, or to have its output multiplexed onto a common output bus. When disabled, the output assumes a high-impedance state.

**INA327 PIN 5**

Pin 5 of the INA327 should be connected to V+ to ensure proper operation.

**DYNAMIC PERFORMANCE**

The typical characteristic “Gain vs Frequency” shows that the INA326 has nearly constant bandwidth regardless of gain. This results from the bandwidth limiting from the recommended filters.

**NOISE PERFORMANCE**

Internal auto-correction circuitry eliminates virtually all 1/f noise (noise that increases at low frequency) in gains of 100 or greater. Noise performance is affected by gain-setting resistor values. Follow recommendations in the “Setting Gain” section for best performance.

Total noise is a combination of input stage noise and output stage noise. When referred to the input, the total mid-band noise is:

\[
V_{NI} = 33nV/\sqrt{Hz} + \frac{800nV/\sqrt{Hz}}{G} \tag{5}
\]

The output noise has some 1/f components that affect performance in gains less than 10. See typical characteristic “Input-Referenced Voltage Noise vs Frequency.”

High-frequency noise is created by internal auto-correction circuitry and is highly dependent on the filter characteristics chosen. This may be the dominant source of noise visible when viewing the output on an oscilloscope. Low cutoff frequency filters will provide lowest noise. Figure 3 shows the typical noise performance as a function of cutoff frequency.

**Figure 3. Total Output Noise vs Required Filter Cutoff Frequency.**
Applications sensitive to the spectral characteristics of high-frequency noise may require consideration of the spurious frequencies generated by internal clocking circuitry. "Spurs" occur at approximately 90kHz and its harmonics (see typical characteristic “Input-Referred Ripple Spectrum”) which may be reduced by additional filtering below 1kHz.

Insufficient filtering at pin 5 can cause nonlinearity with large output voltage swings (very near the supply rails). Noise must be sufficiently filtered at pin 5 so that noise peaks do not “hit the rail” and change the average value of the signal. Figure 3 shows guidelines for filter cutoff frequency.

HIGH-FREQUENCY NOISE

C₂ and C₀ form filters to reduce internally generated auto-correction circuitry noise. Filter frequencies can be chosen to optimize the trade-off between noise and frequency response of the application, as shown in Figure 3. The cutoff frequencies of the filters are generally set to the same frequency. Figure 3 shows the typical output noise for four gains as a function of the ~3dB cutoff frequency of each filter response. Small signals may exhibit the addition of internally generated auto-correction circuitry noise at the output. This noise, combined with broadband noise, becomes most evident in higher gains with filters of wider bandwidth.

INPUT BIAS CURRENT RETURN PATH

The input impedance of the INA326 is extremely high—approximately 10¹⁰Ω. However, a path must be provided for the input bias current of both inputs. This input bias current is approximately ±0.2nA. High input impedance means that this input bias current changes very little with varying input voltage.

Input circuitry must provide a path for this input bias current for proper operation. Figure 4 shows provision for an input bias current path in a thermocouple application. Without a bias current path, the inputs will float to an undefined potential and the output voltage may not be valid.

INPUT COMMON-MODE RANGE

Common instrumentation amplifiers do not respond linearly with common-mode signals near the power-supply rails, even if “rail-to-rail” op amps are used. The INA326 uses a unique topology to achieve true rail-to-rail input behavior (see Figure 5, “Inside the INA326”). The linear input voltage range of each input terminal extends to 20mV below the negative rail, and 100mV above the positive rail.

INPUT PROTECTION

The inputs of the INA326 are protected with internal diodes connected to the power-supply rails. These diodes will clamp the applied signal to prevent it from damaging the input circuitry. If the input signal voltage can exceed the power supplies by more than 0.5V, the input signal current should be limited to less than 10mA to protect the internal clamp diodes. This can generally be done with a series input resistor. Some signal sources are inherently current-limited and do not require limiting resistors.

FILTERING

Filtering can be adjusted through selection of R₂C₂ and R₀C₀ for the desired trade-off of noise and bandwidth. Adjustment of these components will result in more or less ripple due to auto-correction circuitry noise and will also affect broadband noise. Filtering limits slew rate, settling time, and output overload recovery time.

It is generally desirable to keep the resistance of R₀ relatively low to avoid DC gain error created by the subsequent stage loading. This may result in relatively high values for C₀ to produce the desired filter response. The impedance of R₀C₀ can be scaled higher to produce smaller capacitor values if the load impedance is very high.

Certain capacitor types greater than 0.1µF may have dielectric absorption effects that can significantly increase settling time in high-accuracy applications (settling to 0.01%). Polypropylene, polystyrene, and polycarbonate types are generally good. Certain “high-K” ceramic types may produce slow settling “tails.” Settling time to 0.1% is not generally affected by high-K ceramic capacitors. Electrolytic types are not recommended for C₂ and C₀.
The INA326 uses a new, unique internal circuit topology that provides true rail-to-rail input. Unlike other instrumentation amplifiers, it can linearly process inputs up to 20mV below the negative power-supply rail, and 100mV above the positive power-supply rail. Conventional instrumentation amplifier circuits cannot deliver such performance, even if rail-to-rail op amps are used.

The ability to reject common-mode signals is derived in most instrumentation amplifiers through a combination of amplifier CMR and accurately matched resistor ratios. The INA326 converts the input voltage to a current. Current-mode signal processing provides rejection of common-mode input voltage and power-supply variation without accurately matched resistors.

A simplified diagram shows the basic circuit function. The differential input voltage, \((V_{IN+} - V_{IN-})\) is applied across \(R_1\). The signal-generated current through \(R_1\) comes from A1 and A2’s output stages. A2 combines the current in \(R_1\) with a mirrored replica of the current from A1. The resulting current in A2’s output and associated current mirror is two times the current in \(R_1\). This current flows in (or out) of pin 5 into \(R_2\). The resulting gain equation is:

\[
G = 2 \frac{R_2}{R_1}
\]

Amplifiers A1, A2, and their associated mirrors are powered from internal charge-pumps that provide voltage supplies that are beyond the positive and negative supply rails. As a result, the voltage developed on \(R_2\) can actually swing 20mV below the negative power-supply rail, and 100mV above the positive supply rail. A3 provides a buffered output of the voltage on \(R_2\). A3’s input stage is also operated from the charge-pumped power supplies for true rail-to-rail operation.

FIGURE 5. Simplified Circuit Diagram.
APPLICATION CIRCUITS


\[
G = \frac{2 (R_2 \ || \ R'_2)}{R_1}
\]

R_2 and R'_2 are chosen to create a small output offset voltage (e.g., 100mV). Gain is determined by the parallel combination of R_2 and R'_2.

FIGURE 7. Output Referenced to V_{REF}/2.

\[
G = \frac{2(200k\Omega \ || \ 200k\Omega)}{2k\Omega} = 100
\]

FIGURE 8. High-Side Current Shunt Measurement.

\[
V_O = 2(I_L \times R_S) - \frac{R_2}{R_1}
\]

NOTE: Connection point of V+ will include (-----) or exclude (---) quiescent current in the measurement as desired. Output offset required for measurements near zero (see Figure 6).

R_S must be chosen so that the input voltage does not exceed 100mV beyond the rail.

INA326, INA327

SBOS222D

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NOTE: Connection point of $V_{-}$ will include (____) or exclude (---) quiescent current in the measurement as desired. Output offset required for measurements near zero (see Figure 6).

$R_S$ must be chosen so that the input voltage does not exceed 20mV beyond the rail.

$V_O = 2(I_L \times R_S)$


NOTE: 0.2% accuracy. Current shunt monitor circuit can be designed for $-250V$ supply with appropriate selection of high-voltage FET.

$V_S = 0mV$ to $50mV$ max


$V_O = 0.1V$ to $4.9V$
FIGURE 12. Output Offset Adjustment.


NOTE: (1) R₂, R₆, and R₈ could be a single, shared resistor to save board space.

FIGURE 14. Output from Pin 5 to Allow Swing Beyond the Rail.

NOTES: (1) NC denotes No Connection.
(2) Typical swing capability −20mV to (+5V + 100mV).


NOTE: Output resistance is typically 800MΩ.
Resolution < 5nA. Recommended values of Cᵢ = 1nF to 1µF.
FIGURE 16. Programmable ±5mA Current Source.

\[ I_{OUT} = \frac{(V_{REF} - V_{DAC})}{200k\Omega} \left(1 + \frac{10k\Omega}{49.9\Omega}\right) \]

\[ I_o = \pm5mA \text{ with } 0.1\mu A \text{ stability.} \]

FIGURE 17. ±27V Output at 200mA Amplifier with 100µV Offset.

NOTES: (1) The OPA551 is a 60V op amp. (2) The INA326 does not require a negative supply to correct for negative \( V_{OS} \) values from the high-voltage op amp. (3) Voltage offset contribution of \( I_b \) (OPA551) is 100pA \times 2k\Omega = 0.2\mu V. 

Internal charge pump in the INA326 allows this node to swing 20mV below ground without a negative supply.
### PACKAGING INFORMATION

<table>
<thead>
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<th>Orderable Device</th>
<th>Status</th>
<th>Package Type</th>
<th>Package Drawing</th>
<th>Pins</th>
<th>Package Qty</th>
<th>Eco Plan (2)</th>
<th>Lead finish/ Ball material</th>
<th>MSL Peak Temp (3)</th>
<th>Op Temp (°C)</th>
<th>Device Marking (4/5)</th>
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<td>B27</td>
<td>Samples</td>
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</tbody>
</table>

(1) The marketing status values are defined as follows:

**ACTIVE:** Product device recommended for new designs.

**LIFEBUY:** TI has announced that the device will be discontinued, and a lifetime-buy period is in effect.

**NRND:** Not recommended for new designs. Device is in production to support existing customers, but TI does not recommend using this part in a new design.

**PREVIEW:** Device has been announced but is not in production. Samples may or may not be available.

**OBSOLETE:** TI has discontinued the production of the device.

(2) **RoHS:** TI defines "RoHS" to mean semiconductor products that are compliant with the current EU RoHS requirements for all 10 RoHS substances, including the requirement that RoHS substance do not exceed 0.1% by weight in homogeneous materials. Where designed to be soldered at high temperatures, "RoHS" products are suitable for use in specified lead-free processes. TI may reference these types of products as "Pb-Free".

**RoHS Exempt:** TI defines "RoHS Exempt" to mean products that contain lead but are compliant with EU RoHS pursuant to a specific EU RoHS exemption.

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(3) **MSL, Peak Temp.** - The Moisture Sensitivity Level rating according to the JEDEC industry standard classifications, and peak solder temperature.

(4) There may be additional marking, which relates to the logo, the lot trace code information, or the environmental category on the device.

(5) Multiple Device Markings will be inside parentheses. Only one Device Marking contained in parentheses and separated by a "~" will appear on a device. If a line is indented then it is a continuation of the previous line and the two combined represent the entire Device Marking for that device.
Lead finish/Ball material - Orderable Devices may have multiple material finish options. Finish options are separated by a vertical ruled line. Lead finish/Ball material values may wrap to two lines if the finish value exceeds the maximum column width.

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### TAPE AND REEL INFORMATION

#### REEL DIMENSIONS

![Reel Dimensions Diagram](image)

#### TAPE DIMENSIONS

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*All dimensions are nominal.*
### TAPE AND REEL BOX DIMENSIONS

*All dimensions are nominal*

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NOTES:

1. All linear dimensions are in millimeters. Any dimensions in parenthesis are for reference only. Dimensioning and tolerancing per ASME Y14.5M.
2. This drawing is subject to change without notice.
3. This dimension does not include mold flash, protrusions, or gate burrs. Mold flash, protrusions, or gate burrs shall not exceed 0.15 mm per side.
4. This dimension does not include interlead flash. Interlead flash shall not exceed 0.25 mm per side.
5. Reference JEDEC registration MO-187, variation BA.
6. Publication IPC-7351 may have alternate designs.
7. Solder mask tolerances between and around signal pads can vary based on board fabrication site.
NOTES: (continued)

8. Laser cutting apertures with trapezoidal walls and rounded corners may offer better paste release. IPC-7525 may have alternate design recommendations.

9. Board assembly site may have different recommendations for stencil design.
NOTES:  
A. All linear dimensions are in millimeters.  
B. This drawing is subject to change without notice.  
C. Body length does not include mold flash, protrusions, or gate burrs. Mold flash, protrusions, or gate burrs shall not exceed 0.15 per end.  
D. Body width does not include interlead flash. Interlead flash shall not exceed 0.50 per side.  
E. Falls within JEDEC MO-187 variation AA, except interlead flash.
NOTES:
A. All linear dimensions are in millimeters.
B. This drawing is subject to change without notice.
C. Publication IPC–7351 is recommended for alternate designs.
D. Laser cutting apertures with trapezoidal walls and also rounding corners will offer better paste release. Customers should contact their board assembly site for stencil design recommendations. Refer to IPC–7525 for other stencil recommendations.
E. Customers should contact their board fabrication site for solder mask tolerances between and around signal pads.
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