



40-mW STEREO AUDIO POWER AMPLIFIER

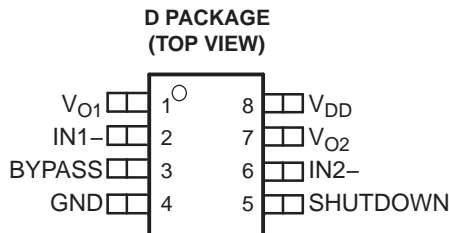
FEATURES

- 40-mW Stereo Output
- PC Power Supply Compatible
 - Fully Specified for 3.3-V and 5-V Operation
- Pop Reduction Circuitry
- Internal Midrail Generation
- Thermal and Short-Circuit Protection
- Surface-Mount Packaging
 - SOIC

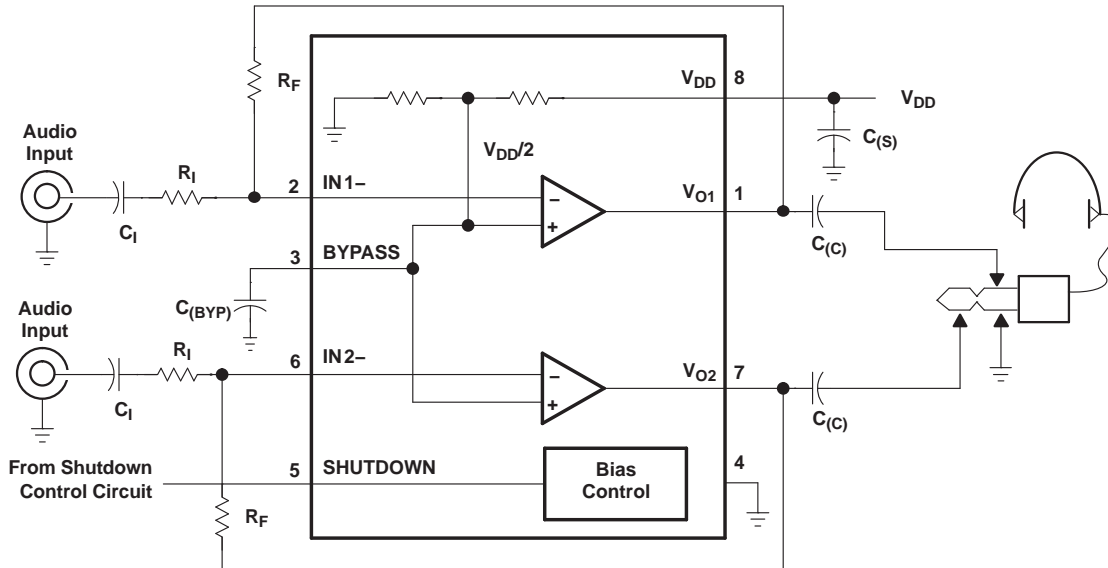
DESCRIPTION

The TPA6113A2 is a stereo audio power amplifier packaged in an 8-pin SOIC package capable of delivering 40 mW of continuous RMS power per channel into 16-Ω loads. Amplifier gain is externally configured by means of two resistors per input channel and does not require external compensation for settings of 0 to 20 dB.

THD+N, when driving a 16-Ω load from 5 V, is 0.03% at 1 kHz, and less than 1% across the audio band of 20 Hz to 20 kHz. For 32-Ω loads, the THD+N is reduced to less than 0.02% at 1 kHz, and is less than 1% across the audio band of 20 Hz to 20 kHz.



TYPICAL APPLICATION CIRCUIT



Please be aware that an important notice concerning availability, standard warranty, and use in critical applications of Texas Instruments semiconductor products and disclaimers thereto appears at the end of this data sheet.



These devices have limited built-in ESD protection. The leads should be shorted together or the device placed in conductive foam during storage or handling to prevent electrostatic damage to the MOS gates.

AVAILABLE OPTIONS

T_A	PACKAGED DEVICES
	SMALL OUTLINE⁽¹⁾ (D)
–40°C to 85°C	TPA6113A2D

(1) The D package is available in left-ended tape and reel only (e.g., TPA6113A2DR).

Terminal Functions

TERMINAL NAME	NO.	I/O	DESCRIPTION
BYPASS	3	I	Tap to voltage divider for internal mid-supply bias supply. Connect to a 0.1- μ F to 1- μ F low ESR capacitor for best performance.
GND	4	I	GND is the ground connection.
IN1–	2	I	IN1– is the inverting input for channel 1.
IN2–	6	I	IN2– is the inverting input for channel 2.
SHUTDOWN	5	I	Puts the device in a low quiescent current mode when held high
V_{DD}	8	I	V_{DD} is the supply voltage terminal.
V_{O1}	1	O	V_{O1} is the audio output for channel 1.
V_{O2}	7	O	V_{O2} is the audio output for channel 2.

ABSOLUTE MAXIMUM RATINGS

over operating free-air temperature range (unless otherwise noted) ⁽¹⁾

	UNIT
V_{DD} Supply voltage	6 V
V_I Input voltage	–0.3 V to $V_{DD} + 0.3$ V
Continuous total power dissipation	internally limited
T_J Operating junction temperature range	–40°C to 150°C
T_{stg} Storage temperature range	–65°C to 150°C
Lead temperature 1,6 mm (1/16 inch) from case for 10 seconds	260°C

(1) Stresses beyond those listed under "absolute maximum ratings" may cause permanent damage to the device. These are stress ratings only, and functional operation of the device at these or any other conditions beyond those indicated under "recommended operating conditions" is not implied. Exposure to absolute-maximum-rated conditions for extended periods may affect device reliability.

DISSIPATION RATING TABLE

PACKAGE	$T_A \leq 25^\circ\text{C}$ POWER RATING	DERATING FACTOR ABOVE $T_A = 25^\circ\text{C}$	$T_A = 70^\circ\text{C}$ POWER RATING	$T_A = 85^\circ\text{C}$ POWER RATING
D	725 mW	5.8 mW/°C	464 mW	377 mW

RECOMMENDED OPERATING CONDITIONS

		MIN	MAX	UNIT
V_{DD}	Supply voltage	2.5	5.5	V
T_A	Operating free-air temperature	–40	85	°C
V_{IH}	High-level input voltage (SHUTDOWN)	60% x V_{DD}		V
V_{IL}	Low-level input voltage (SHUTDOWN)	25% x V_{DD}		V

DC ELECTRICAL CHARACTERISTICS

at $V_{DD} = 3.3$ V, $T_A = 25^\circ\text{C}$ (unless otherwise noted)

PARAMETER	TEST CONDITIONS	MIN	TYP	MAX	UNIT	
V_{OO}	Output offset voltage			10	mV	
PSRR	Power supply rejection ratio	$V_{DD} = 3.2$ V to 3.4 V		70	dB	
I_{DD}	Supply current	SHUTDOWN (pin 5) = 0 V		1.5	3	mA
$I_{DD(SD)}$	Supply current in shutdown mode	SHUTDOWN (pin 5) = V_{DD}		1	10	μA
Z_i	Input impedance			> 1	MΩ	

AC OPERATING CHARACTERISTICS

 $V_{DD} = 3.3$ V, $T_A = 25^\circ\text{C}$, $R_L = 16$ Ω

PARAMETER	TEST CONDITIONS	MIN	TYP	MAX	UNIT
P_O	Output power (each channel)	THD ≤ 0.1%, $f = 1$ kHz		16	mW
THD+N	Total harmonic distortion + noise	$P_O = 16$ mW, 20 Hz – 20 kHz		0.4%	
B_{OM}	Maximum output power BW	G = 20 dB, THD < 5%		> 20	kHz
	Phase margin	Open loop		96°	
	Supply ripple rejection	$f = 1$ kHz, $C_{(BYP)} = 0.47$ F		71	dB
	Channel/channel output separation	$f = 1$ kHz, $P_O = 15$ mW		89	dB
SNR	Signal-to-noise ratio	$P_O = 15$ mW, $A_V = 1$		93	dB
V_n	Noise output voltage	$A_V = 1$		11	μV(rms)

DC ELECTRICAL CHARACTERISTICS

at $V_{DD} = 5.5$ V, $T_A = 25^\circ\text{C}$

PARAMETER	TEST CONDITIONS	MIN	TYP	MAX	UNIT	
V_{OO}	Output offset voltage			10	mV	
PSRR	Power supply rejection ratio	$V_{DD} = 4.9$ V to 5.1 V		70	dB	
I_{DD}	Supply current	SHUTDOWN (pin 5) = 0 V		1.6	3.2	mA
$I_{DD(SD)}$	Supply current in shutdown mode	SHUTDOWN (pin 5) = V_{DD}		1	10	μA
$ I_{IH} $	High-level input current (SHUTDOWN)	$V_{DD} = 5.5$ V, $V_I = V_{DD}$		1	μA	
$ I_{IL} $	Low-level input current (SHUTDOWN)	$V_{DD} = 5.5$ V, $V_I = 0$ V		1	μA	
Z_i	Input impedance			> 1	MΩ	

AC OPERATING CHARACTERISTICS

$V_{DD} = 5\text{ V}$, $T_A = 25^\circ\text{C}$, $R_L = 16\ \Omega$

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
P_O	Output power (each channel)	THD $\leq 0.1\%$, $f = 1\text{ kHz}$		40		mW
THD+N	Total harmonic distortion + noise	$P_O = 20\text{ mW}$, 20 Hz – 20 kHz		0.4%		
B_{OM}	Maximum output power BW	$G = 20\text{ dB}$, THD $< 5\%$		> 20		kHz
	Phase margin	Open loop		96°		
	Supply ripple rejection ratio	$f = 1\text{ kHz}$, $C_{(BYP)} = 0.47\ \mu\text{F}$		61		dB
	Channel/channel output separation	$f = 1\text{ kHz}$, $P_O = 25\text{ mW}$		90		dB
SNR	Signal-to-noise ratio	$P_O = 25\text{ mW}$, $A_V = 1$		94		dB
V_n	Noise output voltage	$A_V = 1$		11.7		$\mu\text{V(rms)}$

AC OPERATING CHARACTERISTICS

$V_{DD} = 3.3\text{ V}$, $T_A = 25^\circ\text{C}$, $R_L = 32\ \Omega$

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
P_O	Output power (each channel)	THD $\leq 0.1\%$, $f = 1\text{ kHz}$		10		mW
THD+N	Total harmonic distortion + noise	$P_O = 10\text{ mW}$, 20 Hz – 20 kHz		0.4%		
B_{OM}	Maximum output power BW	$G = 20\text{ dB}$, THD $< 2\%$		> 20		kHz
	Phase margin	Open loop		96°		
	Supply ripple rejection	$f = 1\text{ kHz}$, $C_{(BYP)} = 0.47\ \text{F}$		71		dB
	Channel/channel output separation	$f = 1\text{ kHz}$, $P_O = 10\text{ mW}$		95		dB
SNR	Signal-to-noise ratio	$P_O = 10\text{ mW}$, $A_V = 1$		94		dB
V_n	Noise output voltage	$A_V = 1$		11		$\mu\text{V(rms)}$

AC OPERATING CHARACTERISTICS

$V_{DD} = 5\text{ V}$, $T_A = 25^\circ\text{C}$, $R_L = 32\ \Omega$

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
P_O	Output power (each channel)	THD $\leq 0.1\%$, $f = 1\text{ kHz}$		90		mW
THD+N	Total harmonic distortion + noise	$P_O = 20\text{ mW}$, 20 Hz – 20 kHz		2%		
B_{OM}	Maximum output power BW	$G = 20\text{ dB}$, THD $< 2\%$		> 20		kHz
	Phase margin	Open loop		97°		
	Supply ripple rejection	$f = 1\text{ kHz}$, $C_{(BYP)} = 0.47\ \mu\text{F}$		61		dB
	Channel/channel output separation	$f = 1\text{ kHz}$, $P_O = 20\text{ mW}$		98		dB
SNR	Signal-to-noise ratio	$P_O = 20\text{ mW}$, $A_V = 1$		97		dB
V_n	Noise output voltage	$A_V = 1$		11.7		$\mu\text{V(rms)}$

TYPICAL CHARACTERISTICS

Table of Graphs

			FIGURE
THD+N	Total harmonic distortion plus noise	vs Frequency	1, 3, 5, 7
		vs Output power	2, 4, 6, 8
	Supply ripple rejection ratio	vs Frequency	9, 10
V_n	Output noise voltage	vs Frequency	11, 12
		Crosstalk	vs Frequency
	Shutdown attenuation	vs Frequency	17, 18
	Output power	vs Load resistance	19
SNR	Signal-to-noise ratio	vs Voltage gain	20

TOTAL HARMONIC DISTORTION + NOISE
vs
FREQUENCY

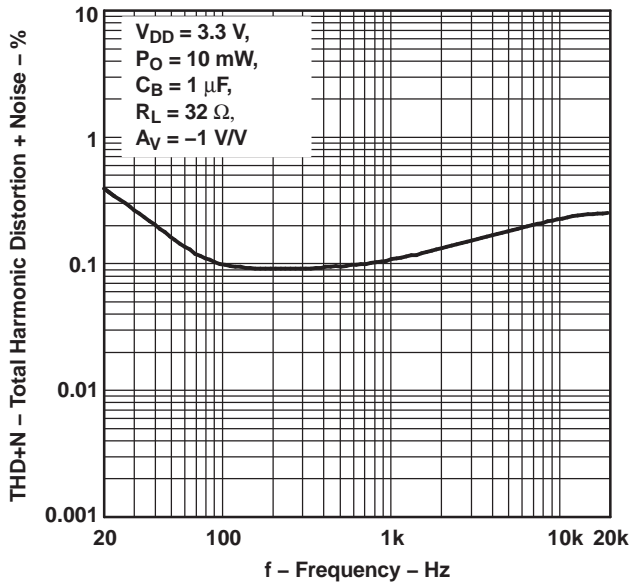


Figure 1.

TOTAL HARMONIC DISTORTION + NOISE
vs
OUTPUT POWER

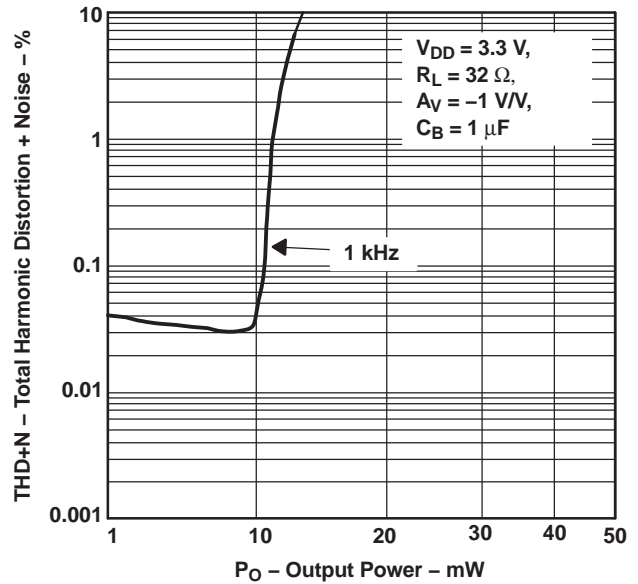


Figure 2.

TOTAL HARMONIC DISTORTION + NOISE
vs
FREQUENCY

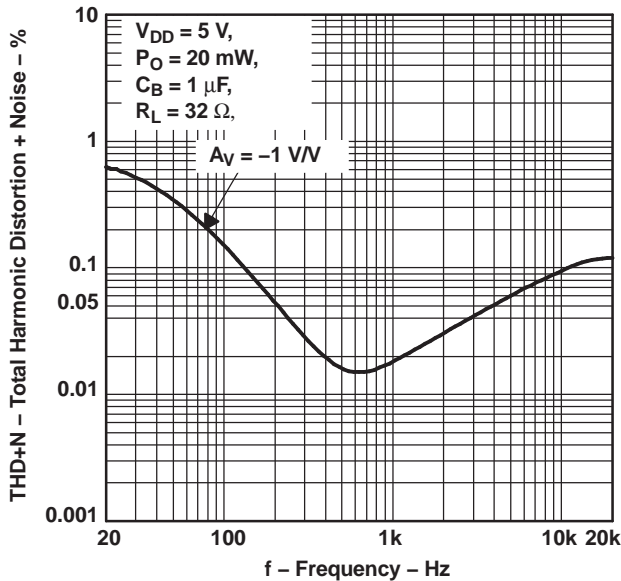


Figure 3.

TOTAL HARMONIC DISTORTION + NOISE
vs
OUTPUT POWER

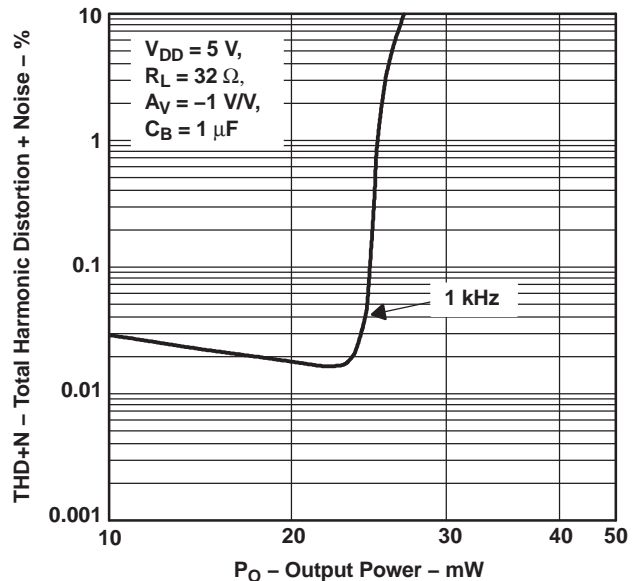


Figure 4.

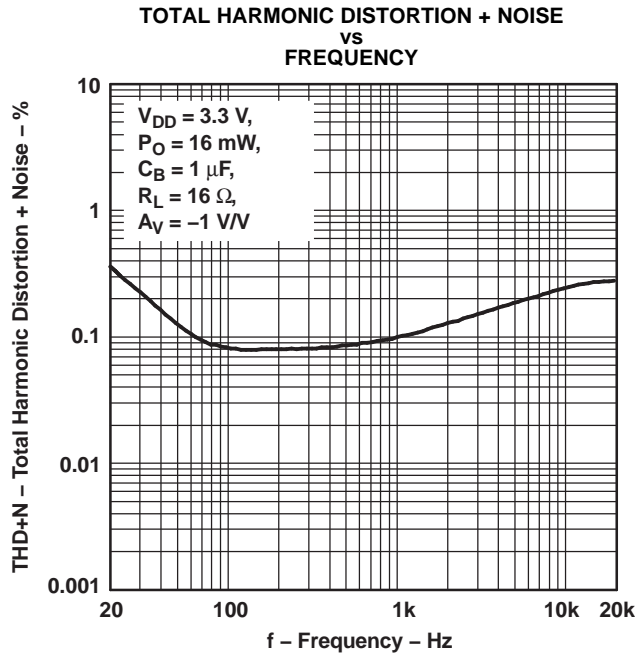


Figure 5.

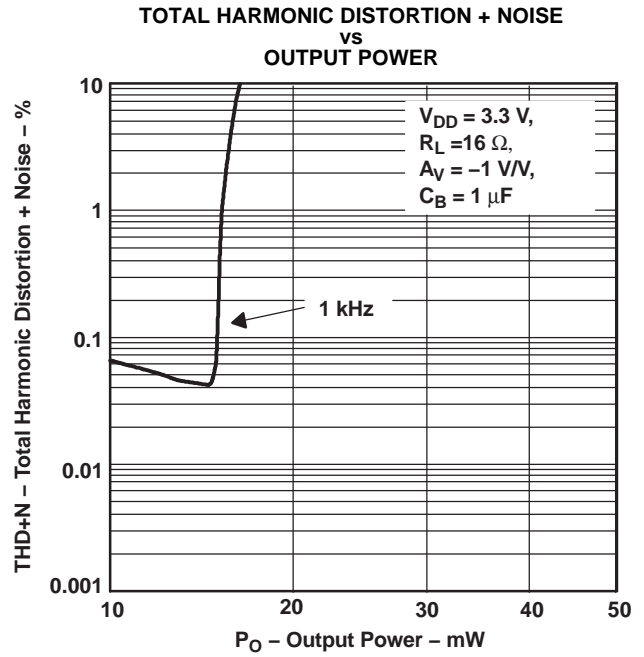


Figure 6.

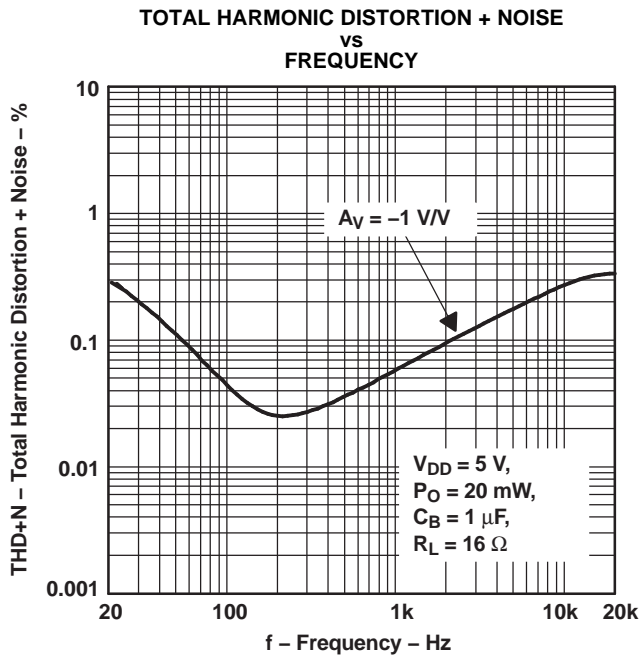


Figure 7.

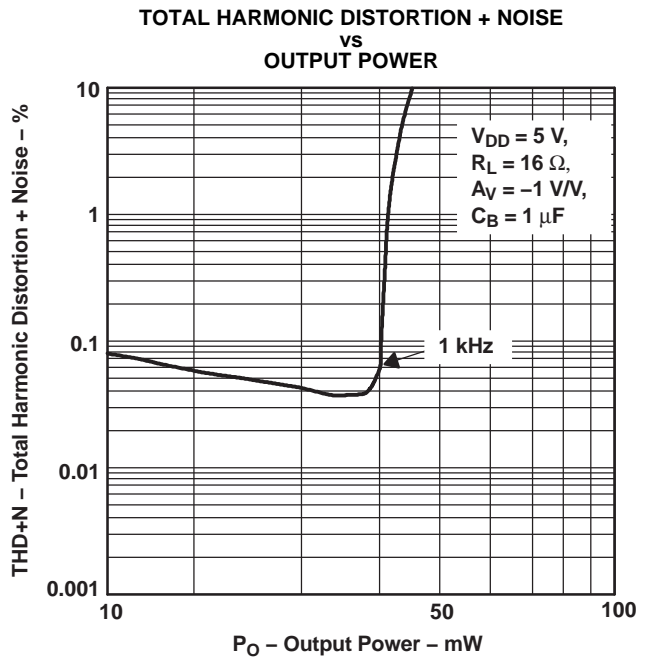
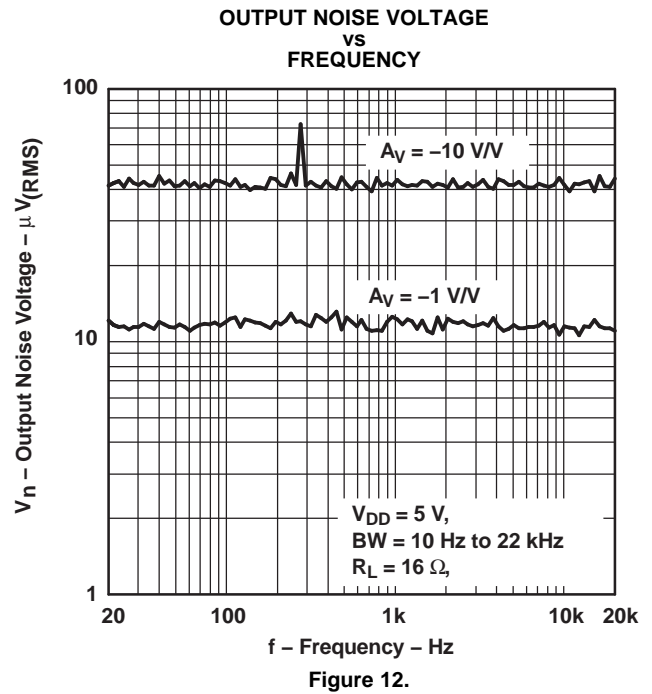
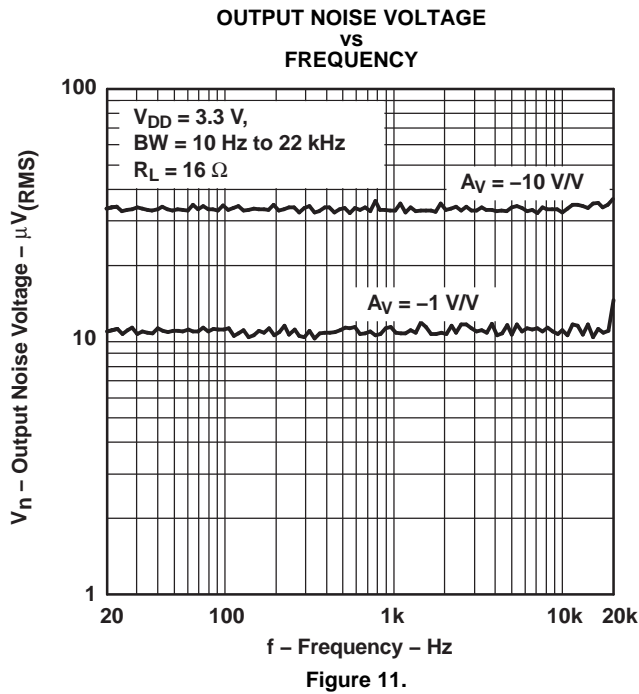
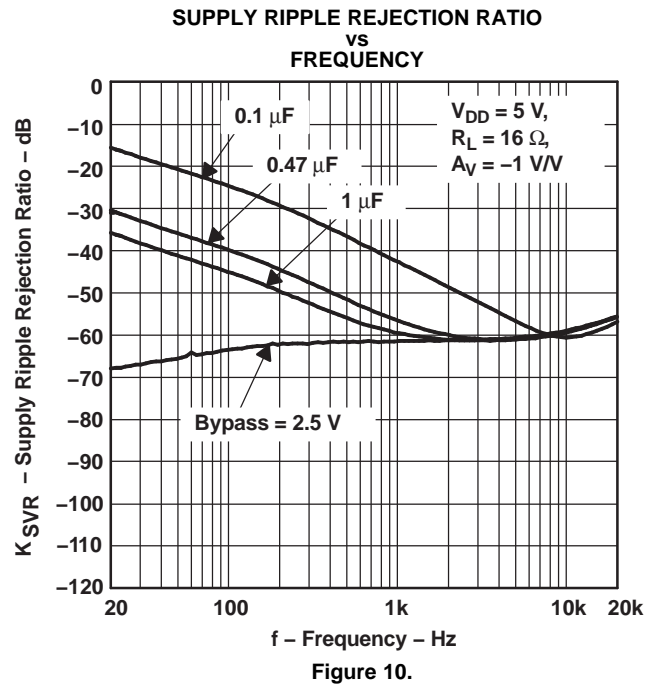
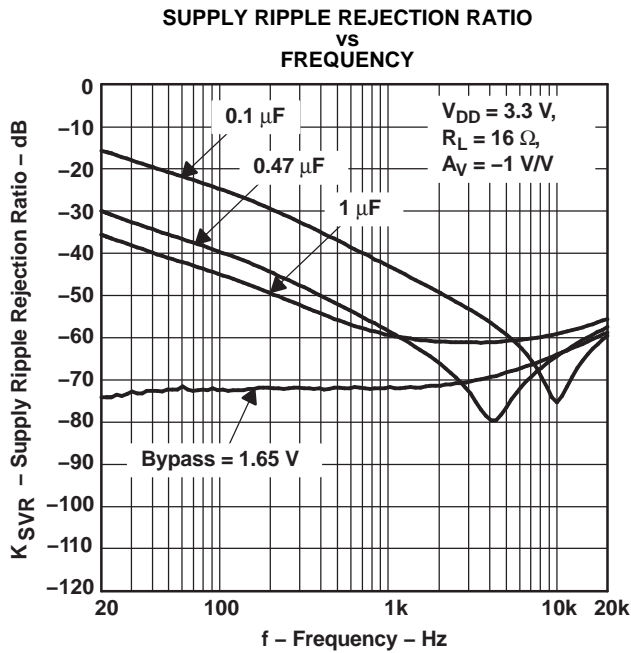


Figure 8.



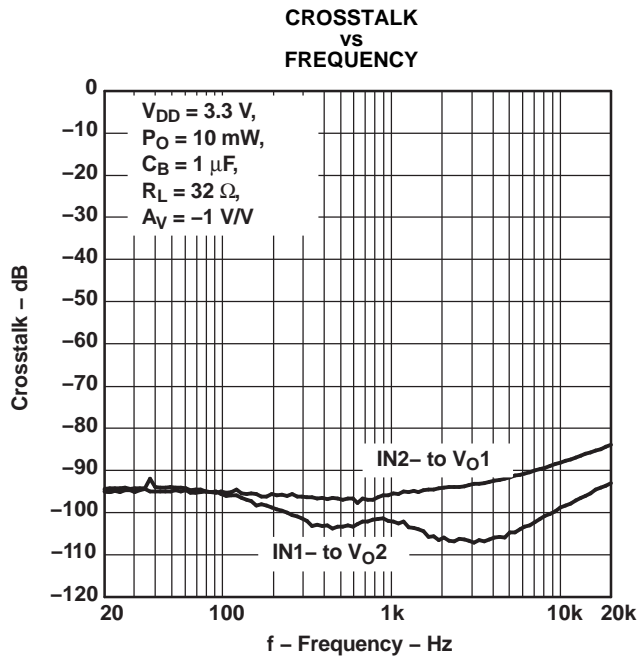


Figure 13.

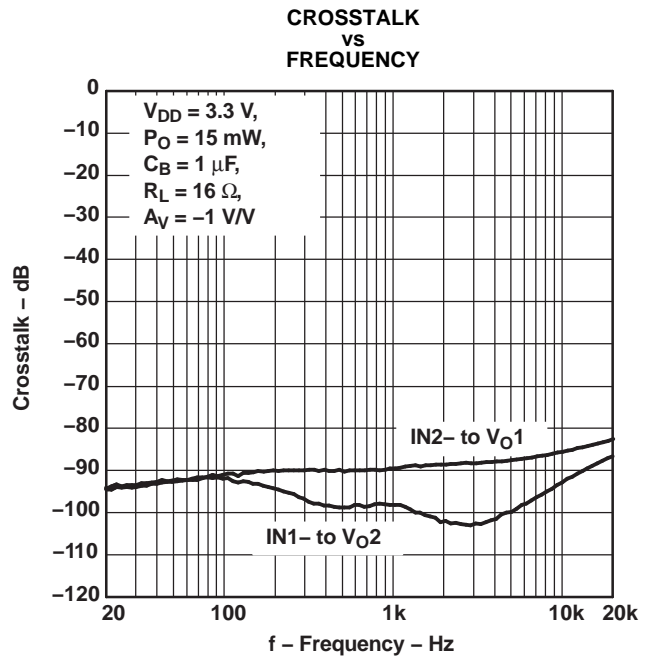


Figure 14.

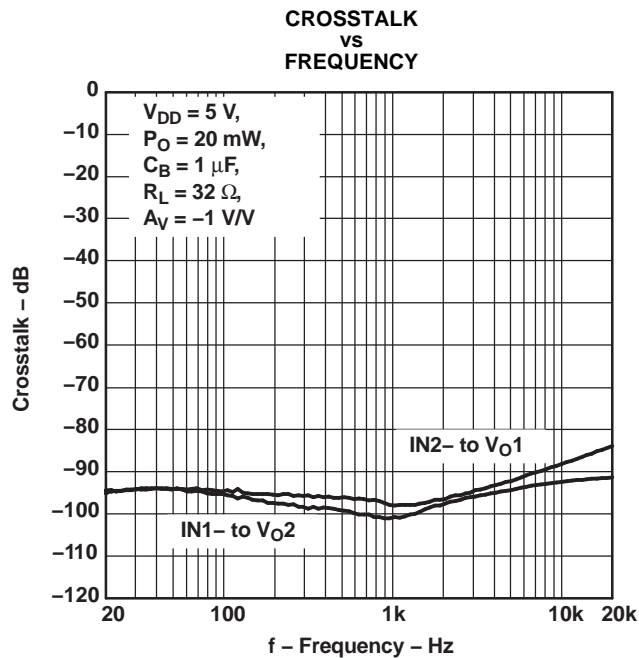


Figure 15.

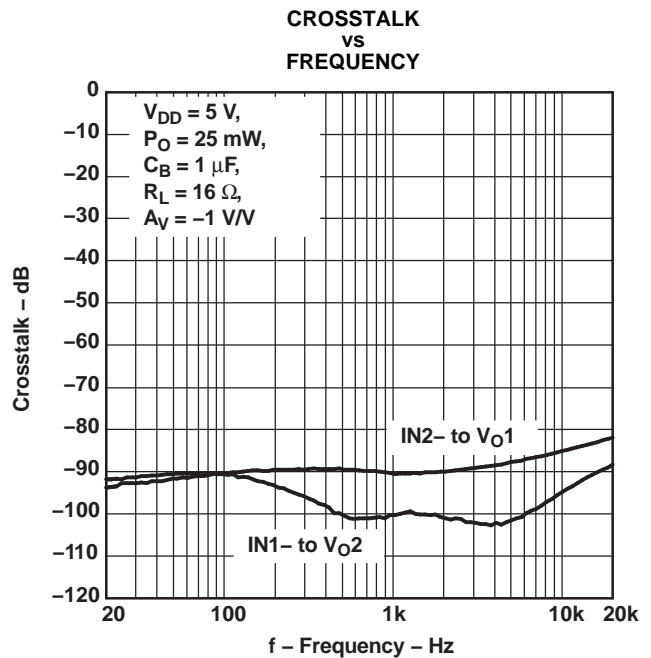


Figure 16.

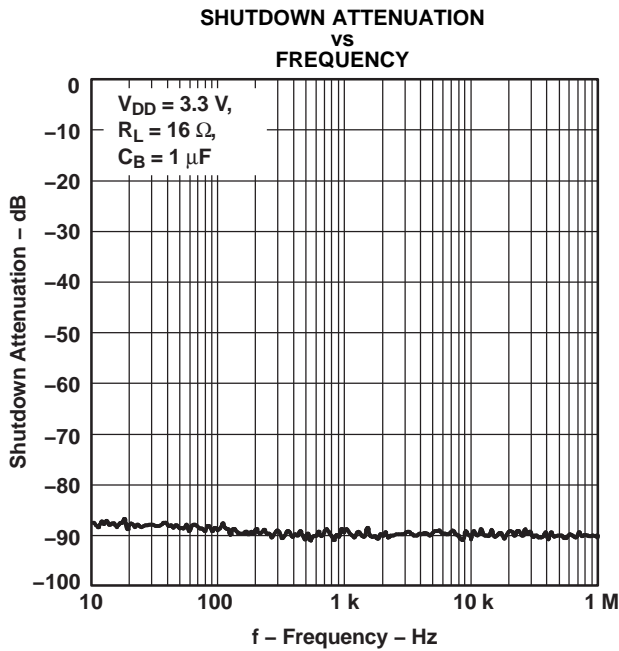


Figure 17.

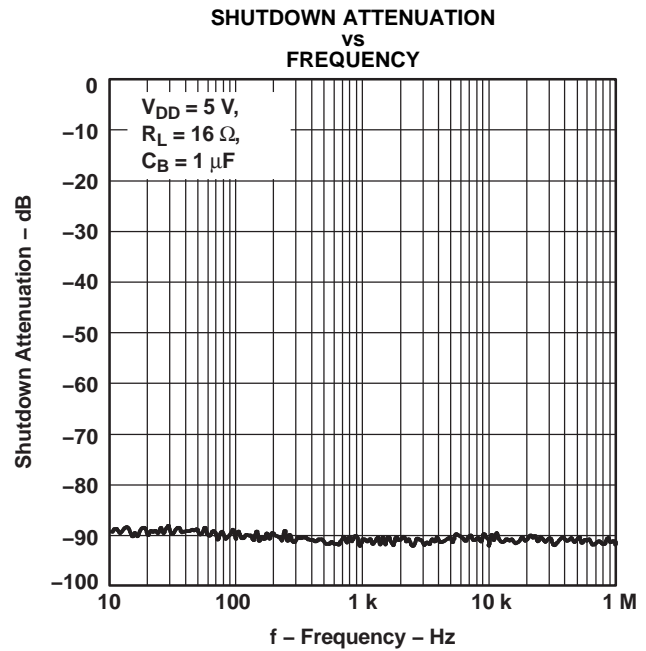


Figure 18.

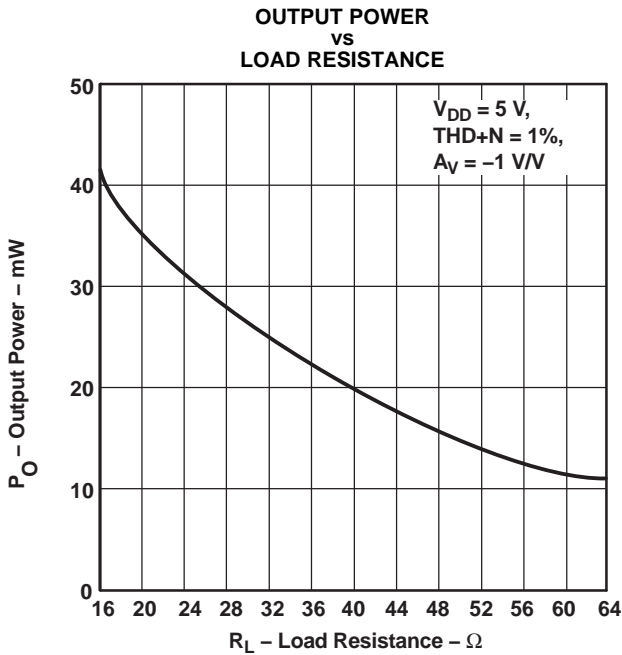


Figure 19.

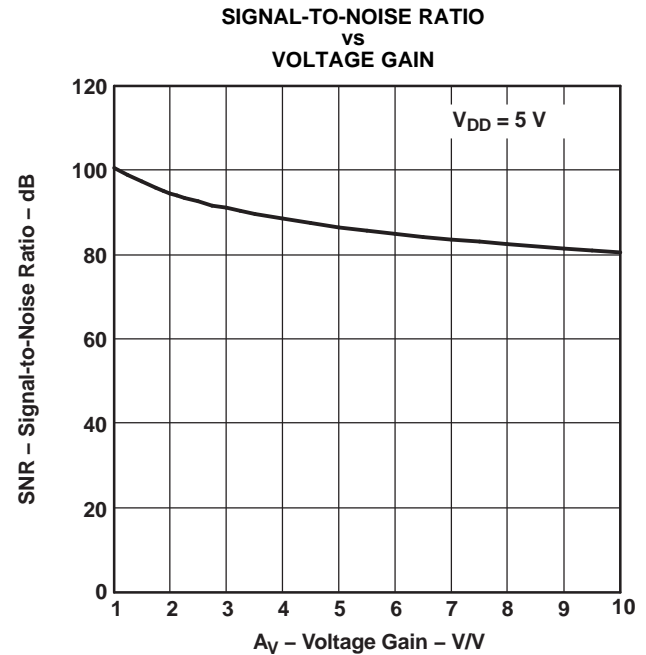


Figure 20.

APPLICATION INFORMATION

GAIN SETTING RESISTORS, R_F and R_I

The gain for the TPA6113A2 is set by resistors R_F and R_I according to [Equation 1](#).

$$\text{Gain} = - \left(\frac{R_F}{R_I} \right) \quad (1)$$

Given that the TPA6113A2 is a MOS amplifier, the input impedance is high. Consequently, input leakage currents are not generally a concern, although noise in the circuit increases as the value of R_F increases. In addition, a certain range of R_F values is required for proper start-up operation of the amplifier. Taken together it is recommended that the effective impedance seen by the inverting node of the amplifier be set between 5 k Ω and 20 k Ω . The effective impedance is calculated in [Equation 2](#).

$$\text{Effective Impedance} = \frac{R_F R_I}{R_F + R_I} \quad (2)$$

As an example, consider an input resistance of 20 k Ω and a feedback resistor of 20 k Ω . The gain of the amplifier would be -1 and the effective impedance at the inverting terminal would be 10 k Ω , which is within the recommended range.

For high-performance applications, metal film resistors are recommended because they tend to have lower noise levels than carbon resistors. For values of R_F above 50 k Ω , the amplifier tends to become unstable due to a pole formed from R_F and the inherent input capacitance of the MOS input structure. For this reason, a small compensation capacitor of approximately 5 pF should be placed in parallel with R_F . In effect, this creates a low-pass filter network with the cutoff frequency defined in [Equation 3](#).

$$f_{c(\text{lowpass})} = \frac{1}{2\pi R_F C_F} \quad (3)$$

For example, if R_F is 100 k Ω and C_F is 5 pF, then $f_{c(\text{lowpass})}$ is 318 kHz, which is well outside the audio range.

INPUT CAPACITOR, C_I

In the typical application, input capacitor C_I is required to allow the amplifier to bias the input signal to the proper dc level for optimum operation. In this case, C_I and R_I form a high-pass filter with the corner frequency determined in [Equation 4](#).

$$f_{c(\text{highpass})} = \frac{1}{2\pi R_I C_I} \quad (4)$$

The value of C_I is important to consider, as it directly affects the bass (low-frequency) performance of the circuit. Consider the example where R_I is 20 k Ω and the specification calls for a flat bass response down to 20 Hz. [Equation 4](#) is reconfigured as [Equation 5](#).

$$C_I = \frac{1}{2\pi R_I f_{c(\text{highpass})}} \quad (5)$$

In this example, C_I is 0.40 μF , so one would likely choose a value in the range of 0.47 μF to 1 μF . A further consideration for this capacitor is the leakage path from the input source through the input network (R_I , C_I) and the feedback resistor (R_F) to the load. This leakage current creates a dc offset voltage at the input to the amplifier that reduces useful headroom, especially in high-gain applications (> 10). For this reason a low-leakage tantalum or ceramic capacitor is the best choice. When polarized capacitors are used, the positive side of the capacitor should face the amplifier input in most applications, as the dc level there is held at $V_{DD}/2$, which is likely higher than the source dc level. Note that it is important to confirm the capacitor polarity in the application.

POWER SUPPLY DECOUPLING, $C_{(S)}$

The TPA6113A2 is a high-performance CMOS audio amplifier that requires adequate power supply decoupling to ensure that the output total harmonic distortion (THD) is as low as possible. Power supply decoupling also prevents oscillations for long lead lengths between the amplifier and the speaker. The optimum decoupling is achieved by using two capacitors of different types that target different types of noise on the power supply leads. For higher frequency transients, spikes, or digital hash on the line, a good low equivalent-series-resistance (ESR) ceramic capacitor, typically 0.1 μF , placed as close as possible to the device V_{DD} lead, works best. For filtering lower frequency noise signals, a larger aluminum electrolytic capacitor of 10 μF or greater placed near the power amplifier is recommended.

MIDRAIL BYPASS CAPACITOR, $C_{(\text{BYP})}$

The midrail bypass capacitor, $C_{(\text{BYP})}$, serves several important functions. During start-up, $C_{(\text{BYP})}$ determines the rate at which the amplifier starts up. This helps to push the start-up pop noise into the subaudible range (so low it cannot be heard). The second function is to reduce noise produced by the power supply caused by coupling into the output drive signal. This noise is from the midrail generation circuit internal to the amplifier. The capacitor is fed from a 230-k Ω source inside the amplifier. To keep the start-up pop as low as possible, the relationship shown in Equation 6 should be maintained.

$$\frac{1}{(C_{(\text{BYP})} \times 230 \text{ k}\Omega)} \leq \frac{1}{(C_1 R_1)} \quad (6)$$

As an example, consider a circuit where $C_{(\text{BYP})}$ is 1 μF , C_1 is 1 μF , and R_1 is 20 k Ω . Inserting these values into Equation 6 results in: $6.25 \leq 50$ which satisfies the rule. Recommended values for bypass capacitor $C_{(\text{BYP})}$ are 0.1 μF to 1 μF , ceramic or tantalum low-ESR, for the best THD and noise performance.

OUTPUT COUPLING CAPACITOR, $C_{(C)}$

In the typical single-supply single-ended (SE) configuration, an output coupling capacitor ($C_{(C)}$) is required to block the dc bias at the output of the amplifier, thus preventing dc currents in the load. As with the input coupling capacitor, the output coupling capacitor and impedance of the load form a high-pass filter governed by Equation 7.

$$f_c = \frac{1}{2\pi R_L C_{(C)}} \quad (7)$$

The main disadvantage, from a performance standpoint, is that the typically small load impedances drive the low-frequency corner higher. Large values of $C_{(C)}$ are required to pass low frequencies into the load. Consider the example where a $C_{(C)}$ of 68 μF is chosen and loads vary from 32 Ω to 47 k Ω . Table 1 summarizes the frequency response characteristics of each configuration.

Table 1. Common Load Impedances vs Low Frequency Output Characteristics in SE Mode

R_L	C_C	LOWEST FREQUENCY
32 Ω	68 μF	73 Hz
10,000 Ω	68 μF	0.23 Hz
47,000 Ω	68 μF	0.05 Hz

As Table 1 indicates, headphone response is adequate and drive into line level inputs (a home stereo for example) is good.

The output coupling capacitor required in single-supply SE mode also places additional constraints on the selection of other components in the amplifier circuit. With the rules described earlier still valid, add the following relationship:

$$\frac{1}{(C_{(BYP)} \times 230 \text{ k}\Omega)} \leq \frac{1}{(C_I R_I)} \ll \frac{1}{R_L C_{(C)}} \quad (8)$$

USING LOW-ESR CAPACITORS

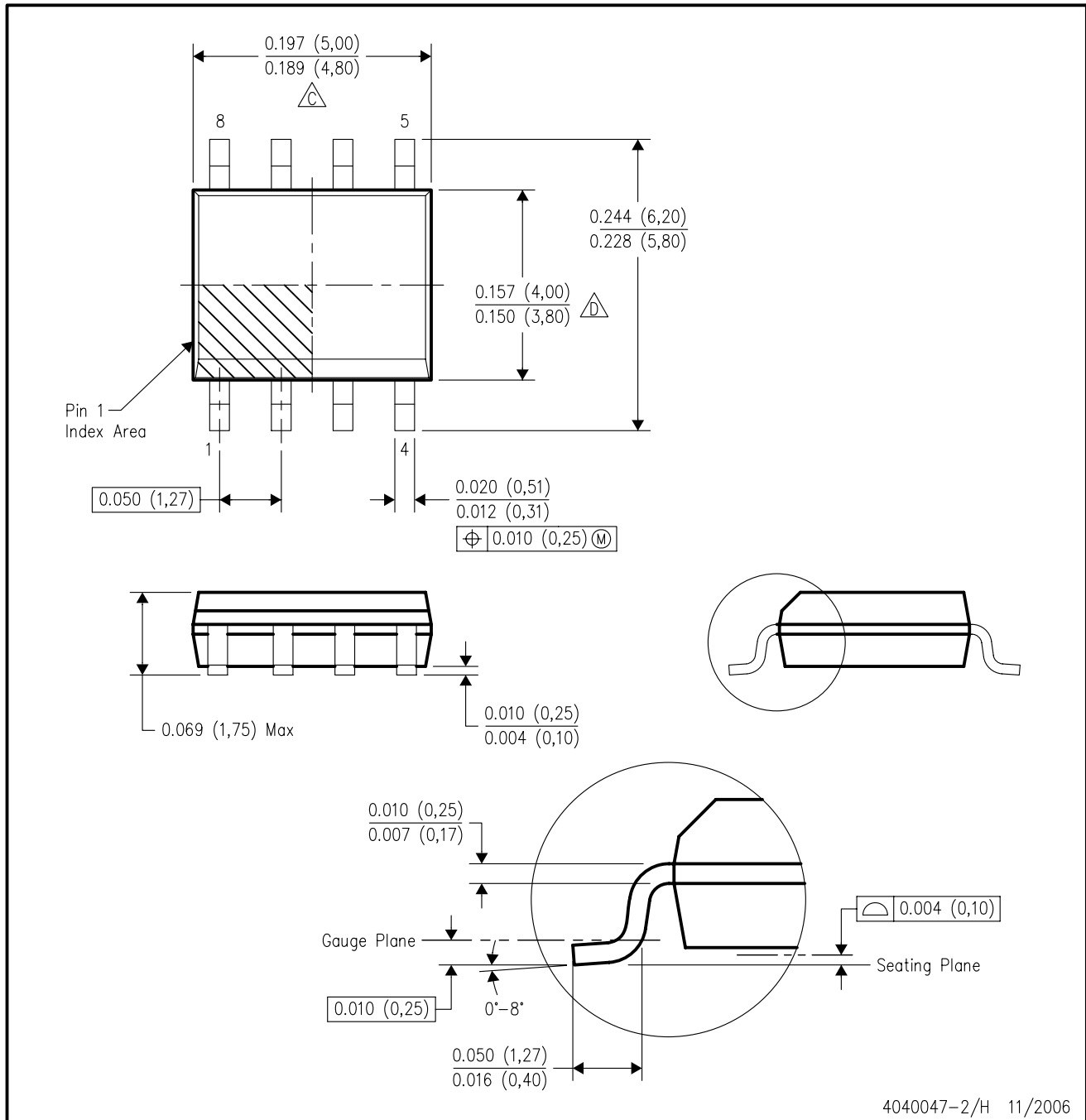
Low-ESR capacitors are recommended throughout this application. A real capacitor can be modeled simply as a resistor in series with an ideal capacitor. The voltage drop across this resistor minimizes the beneficial effects of the capacitor in the circuit. The lower the equivalent value of this resistance, the more the real capacitor behaves like an ideal capacitor.

5-V VERSUS 3.3-V OPERATION

The TPA6113A2 was designed for operation over a supply range of 2.5 V to 5.5 V. This data sheet provides full specifications for 5-V and 3.3-V operation, since these are considered to be the two most common standard voltages. There are no special considerations for 3.3-V versus 5-V operation as far as supply bypassing, gain setting, or stability. The most important consideration is that of output power. Each amplifier in the TPA6113A2 can produce a maximum voltage swing of $V_{DD} - 1$ V. This means, for 3.3-V operation, clipping starts to occur when $V_{O(PP)} = 2.3$ V as opposed when $V_{O(PP)} = 4$ V while operating at 5 V. The reduced voltage swing subsequently reduces maximum output power into the load before distortion begins to become significant.

D (R-PDSO-G8)

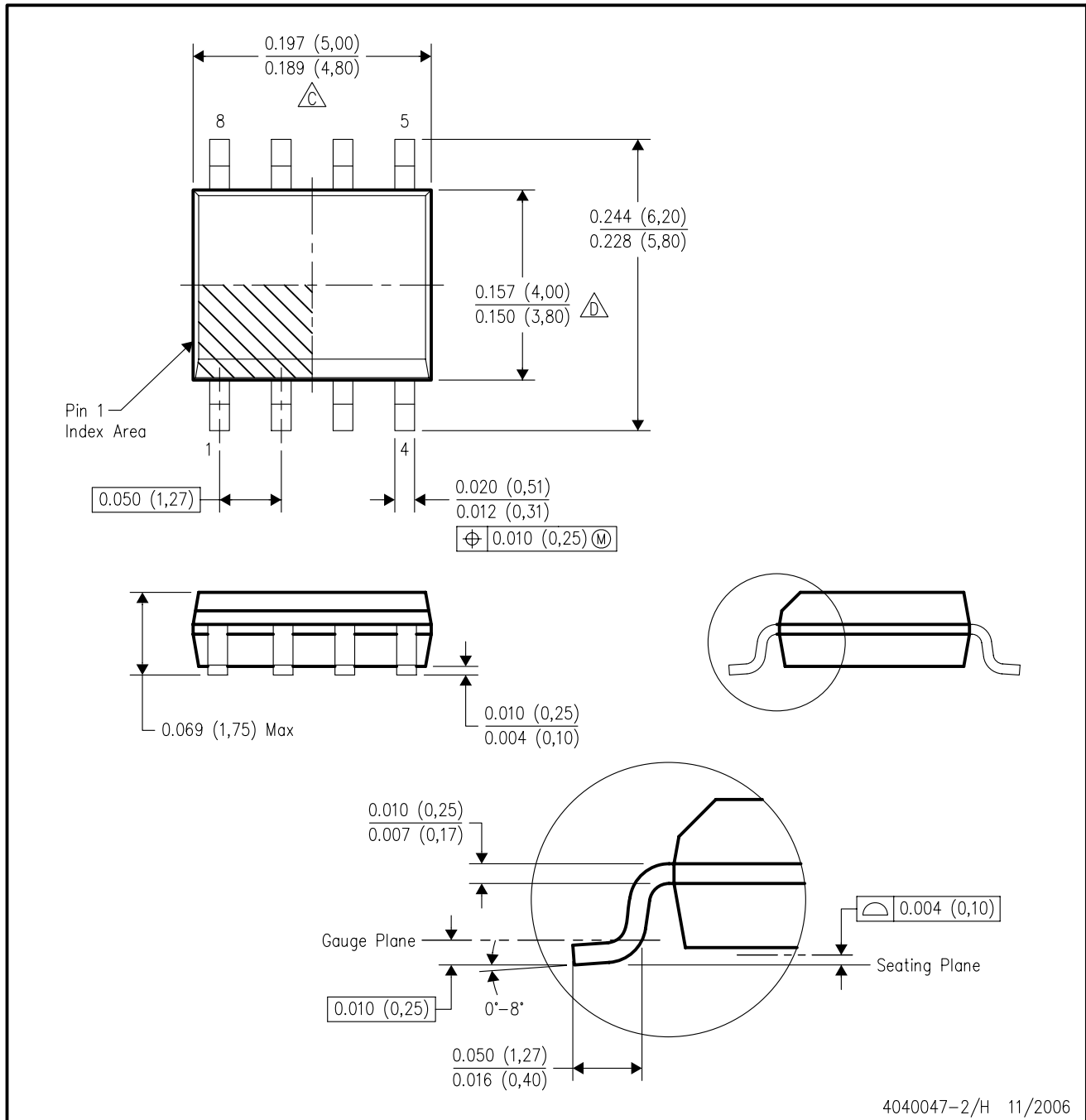
PLASTIC SMALL-OUTLINE PACKAGE



- NOTES:
- A. All linear dimensions are in inches (millimeters).
 - B. This drawing is subject to change without notice.
 - $\triangle C$ Body length does not include mold flash, protrusions, or gate burrs. Mold flash, protrusions, or gate burrs shall not exceed .006 (0,15) per end.
 - $\triangle D$ Body width does not include interlead flash. Interlead flash shall not exceed .017 (0,43) per side.
 - E. Reference JEDEC MS-012 variation AA.

D (R-PDSO-G8)

PLASTIC SMALL-OUTLINE PACKAGE



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