LM25010, LM25010-Q1 42-V, 1-A Step-Down Switching Regulator

1 Features

- LM25010-Q1 Qualified for Automotive Applications
- AEC-Q100 Qualified With the Following Results:
  - Device Temperature Grade 1: –40°C to 125°C Ambient Operating Temperature Range
  - Device Temperature Grade 0: –40°C to 150°C Ambient Operating Temperature Range
  - Device HBM ESD Classification Level 2
  - Device CDM ESD Classification Level C5
- Wide 6-V to 42-V Input Voltage Range
- Valley Current Limiting at 1.25 A
- Programmable Switching Frequency Up To 1 MHz
- Integrated N-Channel Buck Switch
- Integrated High Voltage Bias Regulator
- No Loop Compensation Required
- Ultra-Fast Transient Response
- Nearly Constant Operating Frequency With Line and Load Variations
- Adjustable Output Voltage
- 2.5 V, ±2% Feedback Reference
- Programmable Soft Start
- Thermal Shutdown

2 Applications

- Non-Isolated Telecommunications Regulators
- Secondary Side Post Regulators
- Automotive Electronics

3 Description

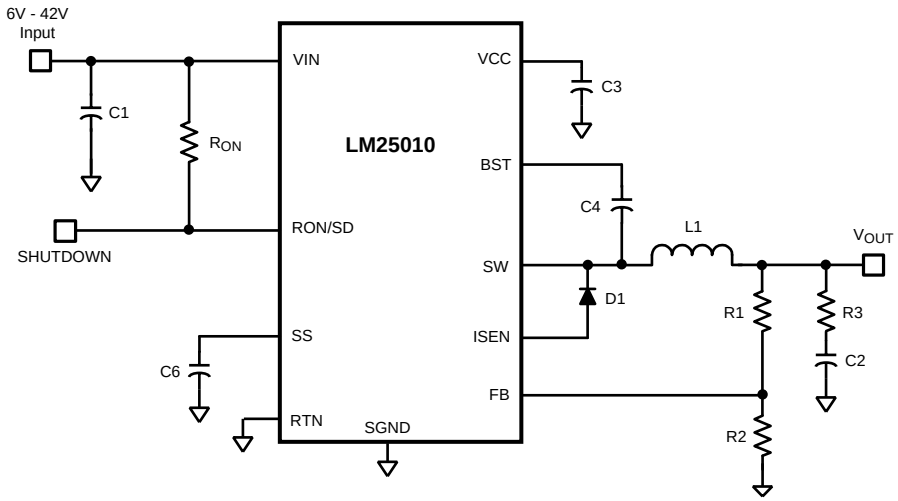
The LM25010 features all the functions needed to implement a low-cost, efficient, buck regulator capable of supplying in excess of 1-A load current. This high voltage regulator integrates an N-Channel Buck Switch, and is available in thermally enhanced 10-pin WSON and 14-pin HTSSOP packages. The constant ON-time regulation scheme requires no loop compensation resulting in fast load transient response and simplified circuit implementation. The operating frequency remains constant with line and load variations due to the inverse relationship between the input voltage and the ON-time. The valley current limit detection is set at 1.25 A. Additional features include: VCC undervoltage lockout, thermal shutdown, gate drive undervoltage lockout, and maximum duty cycle limiter.

Device Information(1)

PART NUMBER	PACKAGE	BODY SIZE (NOM)
LM25010x	WSON (10)	4.00 mm × 4.00 mm
	HTSSOP (14)	4.40 mm × 5.00 mm

(1) For all available packages, see the orderable addendum at the end of the data sheet.

Basic Step-Down Regulator



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4 Revision History

NOTE: Page numbers for previous revisions may differ from page numbers in the current version.

Changes from Revision D (February 2013) to Revision E — **Page**

- Added *Device Information* table, *ESD Ratings* table, *Feature Description* section, *Device Functional Modes* section, *Application and Implementation* section, *Power Supply Recommendations* section, *Layout* section, *Device and Documentation Support* section, and *Mechanical, Packaging, and Orderable Information* section ... 1

Changes from Revision C (February 2013) to Revision D — **Page**

- Changed layout of National Data Sheet to TI format ... 1

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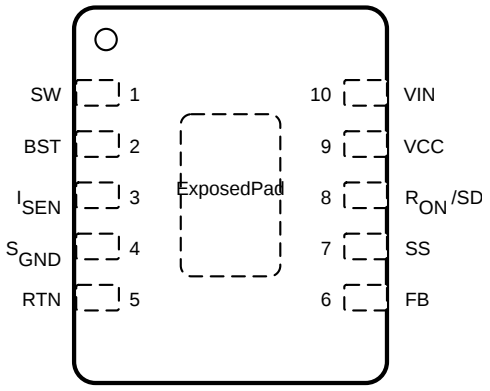
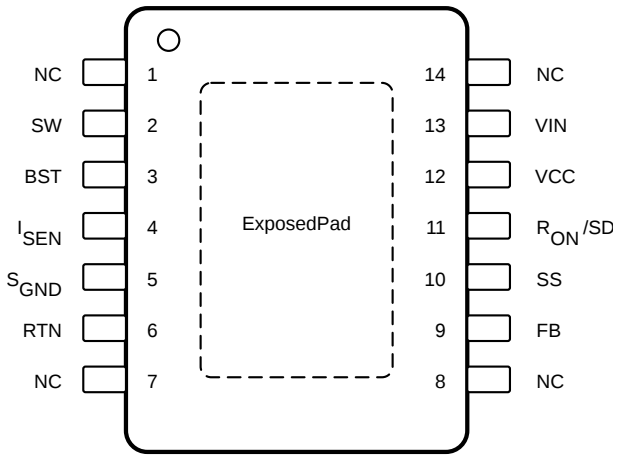
5 Pin Configuration and Functions

DPR Package
10-Pin WSON
Top View



PWP Package
14-Pin HTSSOP
Top View



Pin Functions

PIN			I/O	DESCRIPTION
NAME	WSON	HTSSOP		
BST	2	3	I	Boost pin for bootstrap capacitor. Connect a capacitor from SW to the BST pin. The capacitor is charged from VCC through an internal diode during the buck switch OFF-time.
EP	—	—	—	Exposed metal pad on the underside of the device. It is recommended to connect this pad to the PC board ground plane to aid in heat dissipation.
FB	6	9	I	Voltage feedback input from the regulated output. Input to both the regulation and overvoltage comparators. The FB pin regulation level is 2.5 V.
I_{SEN}	3	4	I	Current sense. During the buck switch OFF-time, the inductor current flows through the internal sense resistor, and out of the I_{SEN} pin to the free-wheeling diode. The current limit comparator keeps the buck switch off if the I_{SEN} current exceeds 1.25 A (typical).
NC	—	1, 7, 8, 14	—	No internal connection. Can be connected to ground plane to improve heat dissipation.
R_{ON}/SD	8	11	I	ON-time control and shutdown. An external resistor from VIN to the R_{ON}/SD pin sets the buck switch ON-time. Grounding this pin shuts down the regulator.
RTN	5	6	—	Ground return for all internal circuitry other than the current sense resistor.
S_{GND}	4	5	—	Current sense ground. Recirculating current flows into this pin to the current sense resistor.
SS	7	10	I	Soft start. An internal 11.5-µA current source charges the SS pin capacitor to 2.5 V to softstart the reference input of the regulation comparator.
SW	1	2	O	Switching node. Internally connected to the buck switch source. Connect to the inductor, free-wheeling diode, and bootstrap capacitor.
VCC	9	12	I	Output of the bias regulator. The voltage at VCC is nominally equal to V_{IN} for V_{IN} < 8.9 V, and regulated at 7 V for V_{IN} > 8.9 V. Connect a 0.47-µF, or larger capacitor from VCC to ground, as close as possible to the pins. An external voltage can be applied to this pin to reduce internal dissipation if V_{IN} is greater than 8.9 V. MOSFET body diodes clamp VCC to V_{IN} if V_{CC} > V_{IN}.
VIN	10	13	I	Input supply. Nominal input range is 6 V to 42 V. Input bypass capacitors should be located as close as possible to the VIN and RTN pins.

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6 Specifications

6.1 Absolute Maximum Ratings

over operating free-air temperature range (unless otherwise noted)(1)

	MIN	MAX	UNIT
VIN to RTN	–0.3	45	V
BST to RTN	–0.3	59	V
SW to RTN (steady state)		–1.5	V
BST to VCC		45	V
BST to SW		14	V
VCC to RTN	–0.3	14	V
SGND to RTN	–0.3	0.3	V
SS to RTN	–0.3	4	V
VIN to SW		45	V
All other inputs to RTN	–0.3	7	V
Lead temperature (soldering, 4 s)(2)		260	°C
Junction temperature, T_J (LM25010, Q1,Q0)	–40	150	°C
Storage temperature, T_{stg}	–65	150	°C

(1) Stresses beyond those listed under *Absolute Maximum Ratings* may cause permanent damage to the device. These are stress ratings only, which do not imply functional operation of the device at these or any other conditions beyond those indicated under *Recommended Operating Ratings*. Exposure to absolute-maximum-rated conditions for extended periods may affect device reliability.
(2) For detailed information on soldering plastic HTSSOP and WSON packages, see *Mechanical, Packaging, and Orderable Information*.

6.2 ESD Ratings: LM25010

			VALUE	UNIT
$V_{(ESD)}$	Electrostatic discharge	Human-body model (HBM), per ANSI/ESDA/JEDEC JS-001(1)	±2000	V
		Charged-device model (CDM), per JEDEC specification JESD22-C101(2)	±750	

(1) JEDEC document JEP155 states that 500-V HBM allows safe manufacturing with a standard ESD control process.
(2) JEDEC document JEP157 states that 250-V CDM allows safe manufacturing with a standard ESD control process.

6.3 ESD Ratings: LM25010-Q1, LM25010-Q0

			VALUE	UNIT
$V_{(ESD)}$	Electrostatic discharge	Human-body model (HBM), per AEC Q100-002(1)(2)	±2000	V
		Charged-device model (CDM), per AEC Q100-011(3)	±750	

(1) AEC Q100-002 indicates that HBM stressing shall be in accordance with the ANSI/ESDA/JEDEC JS-001 specification.
(2) Level listed above is the passing level per ANSI/ESDA/JEDEC JS-001. JEDEC document JEP155 states that 500 V HBM allows safe manufacturing with a standard ESD control process.
(3) Level listed above is the passing level per EIA-JEDEC JESD22-C101. JEDEC document JEP157 states that 250 V CDM allows safe manufacturing with a standard ESD control process.

6.4 Recommended Operating Ratings

over operating free-air temperature range (unless otherwise noted)

			MIN	NOM	MAX	UNIT
V_{IN}	Input voltage		6		42	V
I_O	Output current				1	A
Ext-V_{CC}	External bias voltage		8		13	V
T_J	Junction temperature	LM25010	–40		125	°C
		LM25010-Q1, LM25010-Q0	–40		150	°C

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6.5 Thermal Information

THERMAL METRIC[1]		LM25010, LM25010-Q1		UNIT
		DPR (WSON)	PWP (HTSSOP)	
		10 PINS	14 PINS	
$R_{\theta JA}$	Junction-to-ambient thermal resistance	36	41.1	°C/W
$R_{\theta JC(top)}$	Junction-to-case (top) thermal resistance	31.9	26.5	°C/W
$R_{\theta JB}$	Junction-to-board thermal resistance	13.2	22.5	°C/W
ψ_{JT}	Junction-to-top characterization parameter	0.3	0.7	°C/W
ψ_{JB}	Junction-to-board characterization parameter	13.5	22.2	°C/W
$R_{\theta JC(bot)}$	Junction-to-case (bottom) thermal resistance	3	3.3	°C/W

(1) For more information about traditional and new thermal metrics, see the *Semiconductor and IC Package Thermal Metrics* application report, SPRA953.

6.6 Electrical Characteristics

Typical values correspond to T_J = 25°C, minimum and maximum limits apply over T_J = –40°C to 125°C, V_{IN} = 24 V, and R_{ON} = 200 kΩ (unless otherwise noted).[1][2]

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
V_{CC} REGULATOR						
V_{CC}Reg	VCC regulated output		6.6	7	7.4	V
	V_{IN} - V_{CC}	I_{CC} = 0 mA, F_S ≤ 200 kHz, 6 V ≤ V_{IN} ≤ 8.5 V		100		mV
	V_{CC} bypass threshold	V_{IN} increasing		8.9		V
	V_{CC} bypass hysteresis	V_{IN} decreasing		260		mV
	V_{CC} output impedance (0 mA ≤ I_{CC} ≤ 5 mA)	V_{IN} = 6 V		55		Ω
		V_{IN} = 8 V		50		
		V_{IN} = 24 V		0.21		
	V_{CC} current limit	V_{IN} = 24 V, V_{CC} = 0 V		15		mA
$UVLO_{VCC}$	V_{CC} undervoltage lockout threshold	V_{CC} increasing		5.25		V
	$UVLO_{VCC}$ hysteresis	V_{CC} decreasing		180		mV
	$UVLO_{VCC}$ filter delay	100-mV overdrive		3		µs
	I_{IN} operating current	Non-switching, FB = 3 V		645	920	µA
	I_{IN} shutdown current	R_{ON}/SD = 0 V		90	170	µA
SOFTSTART PIN						
I_{SS}	Internal current source		8	11.5	15	µA
CURRENT LIMIT						
I_{LIM}	Threshold	Current out of I_{SEN}	1	1.25	1.5	A
	Resistance from ISEN to SGND			130		mΩ
	Response time			150		ns
ON TIMER, R_{ON}/SD PIN						
	Shutdown threshold	Voltage at RON/SD rising	0.3	0.7	1.05	V
	Threshold hysteresis			40		mV
REGULATION AND OVER-VOLTAGE COMPARATORS (FB PIN)						
V_{REF}	FB regulation threshold	T_J ≤ 125°C	2.445	2.5	2.55	V
		T_J ≤ 150°C	2.435			
	FB overvoltage threshold			2.9		V
	FB bias current			1		nA

(1) All minimum and maximum limits are specified by correlating the electrical characteristics to process and temperature variations and applying statistical process control.
(2) The junction temperature (T_J in °C) is calculated from the ambient temperature (T_A in °C) and power dissipation (P_D in Watts) as follows: $T_J = T_A + (P_D \times R_{\theta JA})$ where $R_{\theta JA}$ (in °C/W) is the package thermal impedance provided in *Thermal Information*

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Electrical Characteristics (continued)

Typical values correspond to T_J = 25°C, minimum and maximum limits apply over T_J = –40°C to 125°C, V_{IN} = 24 V, and R_{ON} = 200 kΩ (unless otherwise noted).(1)(2)

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
THERMAL SHUTDOWN						
T_{SD}	Thermal shutdown temperature			175		°C
	Thermal shutdown hysteresis			20		°C

6.7 Switching Characteristics

Typical values correspond to T_J = 25°C, minimum and maximum limits apply over T_J = –40°C to 125°C, and V_{IN} = 24 V (unless otherwise noted)(1)

PARAMETER		TEST CONDITIONS		MIN	TYP	MAX	UNIT
$R_{DS(ON)}$	Buck switch	f_{SW} = 200 mA	$T_J \le 125°C$		0.35	0.8	Ω
			$T_J \le 150°C$			0.85	
$UVLO_{GD}$	Gate drive UVLO	V_{BST} - V_{SW} increasing		1.7	3	4	V
	$UVLO_{GD}$ hysteresis				400		mV
OFF TIMER							
t_{OFF}	Minimum OFF-time				260		ns
ON TIMER							
t_{ON} – 1	ON-time	V_{IN} = 10 V, R_{ON} = 200 kΩ		2.1	2.75	3.4	µs
t_{ON} – 2	ON-time	V_{IN} = 42 V, R_{ON} = 200 kΩ		500	695	890	ns

(1) All minimum and maximum limits are specified by correlating the electrical characteristics to process and temperature variations while applying statistical process control.

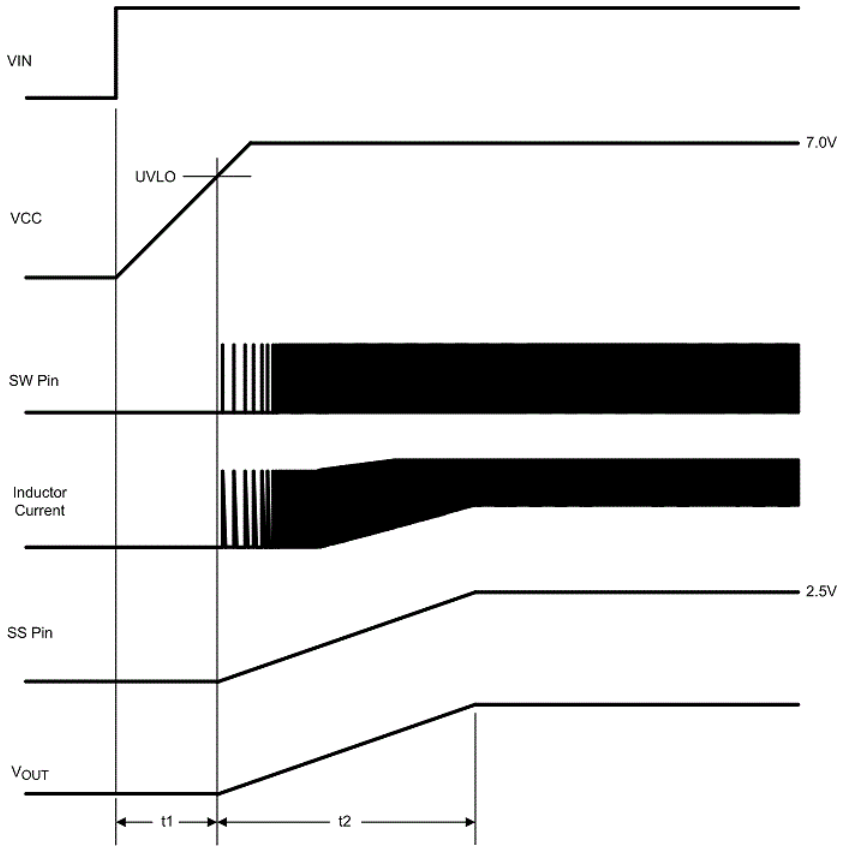

Figure 1. Start-Up Sequence

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6.8 Typical Characteristics

at T_A = 25°C (unless otherwise noted)

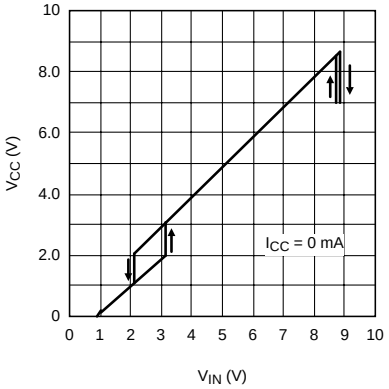


Figure 2. V_{CC} vs V_{IN}

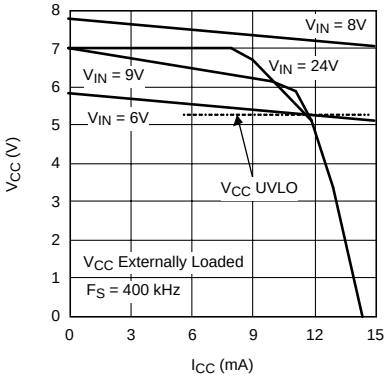


Figure 3. V_{CC} vs I_{CC}

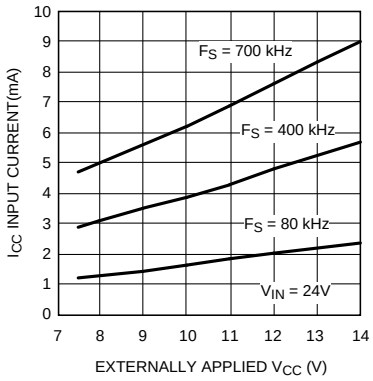


Figure 4. I_{CC} vs Externally Applied V_{CC}

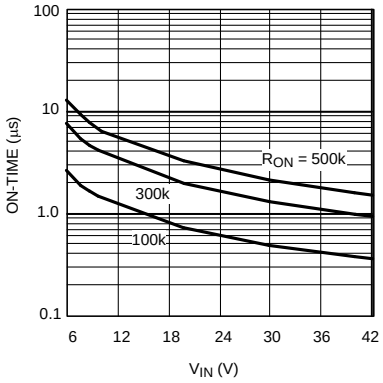


Figure 5. ON-Time vs V_{IN} and R_{ON}

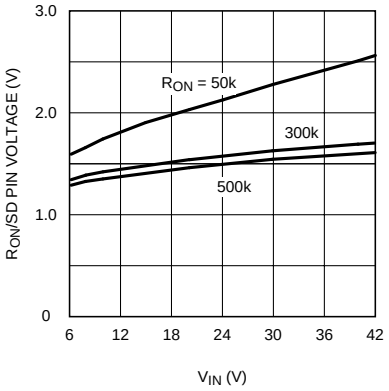


Figure 6. Voltage at RON/SD Pin

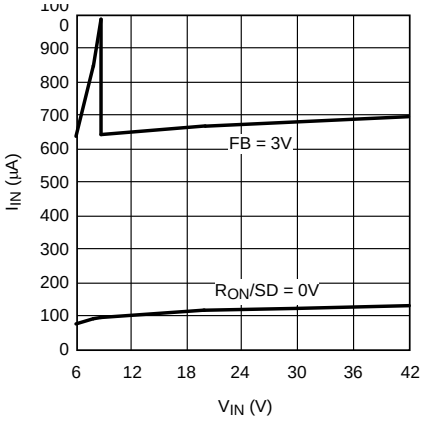


Figure 7. I_{IN} vs V_{IN}

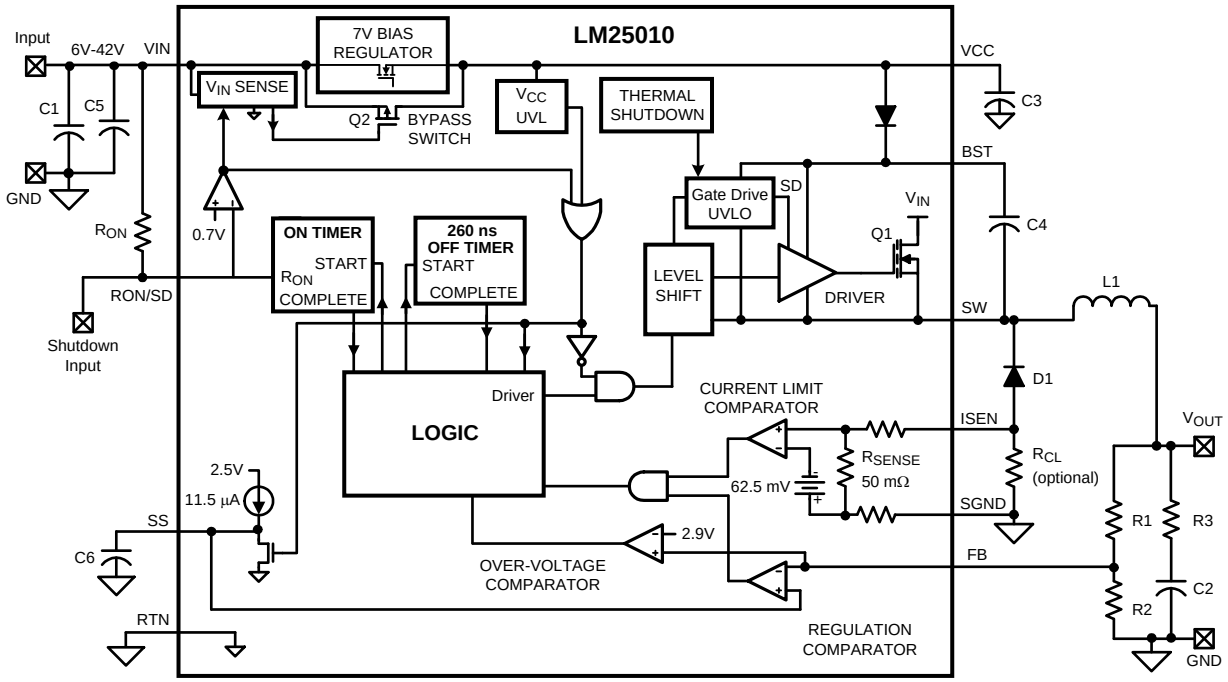
7 Detailed Description

7.1 Overview

The LM25010 step-down switching regulator features all the functions needed to implement a low cost, efficient buck DC-DC converter capable of supplying in excess of 1 A to the load. This high voltage regulator integrates an N-Channel buck switch, with an easy to implement constant ON-time controller. It is available in the thermally enhanced WSON and HTSSOP packages. The regulator compares the feedback voltage to a 2.5-V reference to control the buck switch, and provides a switch ON-time which varies inversely with V_{IN}. This feature results in the operating frequency remaining relatively constant with load and input voltage variations. The switching frequency can range from less than 100 kHz to 1 MHz. The regulator requires no loop compensation resulting in very fast load transient response. The valley current limit circuit holds the buck switch off until the free-wheeling inductor current falls below the current limit threshold, nominally set at 1.25 A.

The LM25010 can be applied in numerous applications to efficiently step-down higher DC voltages. Features include: thermal shutdown, V_{CC} undervoltage lockout, gate drive undervoltage lockout, and maximum duty cycle limit.

7.2 Functional Block Diagram



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7.3 Feature Description

7.3.1 Control Circuit Overview

The LM25010 employs a control scheme based on a comparator and a one-shot ON timer, with the output voltage feedback (FB) compared to an internal reference (2.5 V). If the FB voltage is below the reference the buck switch is turned on for a time period determined by the input voltage and a programming resistor (R_{ON}). Following the ON-time the switch remains off for a fixed 260-ns OFF-time, or until the FB voltage falls below the reference, whichever is longer. The buck switch then turns on for another ON-time period. Referring to the *Functional Block Diagram*, the output voltage is set by R1 and R2. The regulated output voltage is calculated with Equation 1.

$$V_{OUT} = 2.5\ V \times (R1 + R2) / R2 \quad (1)$$

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Feature Description (continued)

The LM25010 requires a minimum of 25-mV of ripple voltage at the FB pin for stable fixed-frequency operation. If the output capacitor's ESR is insufficient, additional series resistance may be required (R3 in the *Functional Block Diagram*).

The LM25010 operates in continuous conduction mode at heavy load currents, and discontinuous conduction mode at light load currents. In continuous conduction mode current always flows through the inductor, never decaying to zero during the OFF-time. In this mode the operating frequency remains relatively constant with load and line variations. The minimum load current for continuous conduction mode is one-half the inductor's ripple current amplitude. Calculate the operating frequency in the continuous conduction mode with Equation 2.

$$F_S = \frac{V_{OUT} \times (V_{IN} - 1.4V)}{1.18 \times 10^{-10} \times (R_{ON} + 1.4\ k\Omega) \times V_{IN}} \quad (2)$$

The buck switch duty cycle is equal to Equation 3.

$$DC = \frac{t_{ON}}{t_{ON} + t_{OFF}} = t_{ON} \times F_S = \frac{V_{OUT}}{V_{IN}} \quad (3)$$

Under light load conditions, the LM25010 operates in discontinuous conduction mode, with zero current flowing through the inductor for a portion of the OFF-time. The operating frequency is always lower than that of the continuous conduction mode, and the switching frequency varies with load current. Conversion efficiency is maintained at a relatively high level at light loads because the switching losses diminish as the power delivered to the load is reduced. Calculate the approximate discontinuous mode operating frequency with Equation 4.

$$F_S = \frac{V_{OUT}^2 \times L1 \times 1.4 \times 10^{20}}{R_L \times R_{ON}^2} \quad (4)$$

where

- R_L = the load resistance

7.3.2 Start-Up Regulator (V_{CC})

A high voltage bias regulator is integrated within the LM25010. The input pin (VIN) can be connected directly to line voltages between 6 V and 42 V. Referring to the *Functional Block Diagram* and the graph of V_{CC} vs V_{IN}, when V_{IN} is between 6 V and the bypass threshold (nominally 8.9 V), the bypass switch (Q2) is on, and V_{CC} tracks V_{IN} within 100 mV to 150 mV. The bypass switch on-resistance is approximately 50 Ω, with inherent current limiting at approximately 100 mA. When VIN is above the bypass threshold, Q2 is turned off, and V_{CC} is regulated at 7 V. The V_{CC} regulator output current is limited at approximately 15 mA. When the LM25010 is shutdown using the RON/SD pin, the V_{CC} bypass switch is shut off, regardless of the voltage at VIN.

When V_{IN} exceeds the bypass threshold, the time required for Q2 to shut off is approximately 2 µs to 3 µs. The capacitor at VCC (C3) must be a minimum of 0.47 µF to prevent the voltage at VCC from rising above its absolute maximum rating in response to a step input applied at VIN. C3 must be located as close as possible to the LM25010 pins.

In applications with a relatively high input voltage, power dissipation in the bias regulator is a concern. An auxiliary voltage of between 7.5 V and 14 V can be diode connected to the VCC pin (D2 in Figure 8) to shut off the VCC regulator, reducing internal power dissipation. The current required into the VCC pin is shown in the Typical Performance Characteristics. Internally a diode connects VCC to VIN requiring that the auxiliary voltage be less than V_{IN}.

The turn-on sequence is shown in Figure 1. When VCC exceeds the undervoltage lockout threshold (UVLO) of 5.25 V (t1 in Figure 1), the buck switch is enabled, and the SS pin is released to allow the softstart capacitor (C6) to charge up. The output voltage V_{OUT} is regulated at a reduced level which increases to the desired value as the softstart voltage increases (t2 in Figure 1).

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Feature Description (continued)

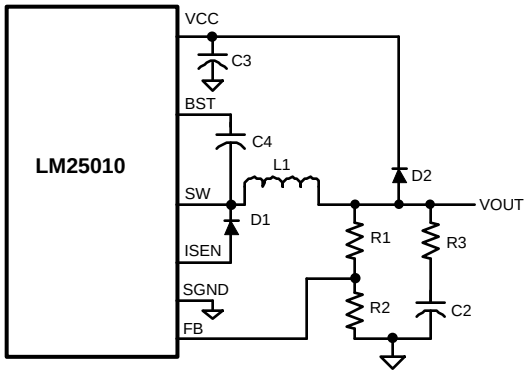

Figure 8. Self-Biased Configuration

7.3.3 Regulation Comparator

The feedback voltage at the FB pin is compared to the voltage at the SS pin (2.5 V, ±2%). In normal operation an ON-time period is initiated when the voltage at FB falls below 2.5 V. The buck switch conducts for the ON-time programmed by R_{ON}, causing the FB voltage to rise above 2.5 V. After the ON-time period the buck switch remains off until the FB voltage falls below 2.5 V. Input bias current at the FB pin is less than 5 nA over temperature.

7.3.4 Overvoltage Comparator

The feedback voltage at FB is compared to an internal 2.9 V reference. If the voltage at FB rises above 2.9 V the ON-time is immediately terminated. This condition can occur if the input voltage, or the output load, changes suddenly. The buck switch remains off until the voltage at FB falls below 2.5 V.

7.3.5 ON-Time Control

The ON-time of the internal buck switch is determined by the R_{ON} resistor and the input voltage (V_{IN}), and is calculated with Equation 5.

$$t_{ON} = \frac{1.18 \times 10^{-10} \times (R_{ON} + 1.4k)}{(V_{IN} - 1.4V)} + 67\ ns \quad (5)$$

The R_{ON} resistor can be determined from the desired ON-time by re-arranging Equation 5 to Equation 6.

$$R_{ON} = \frac{(t_{ON} - 67\ ns) \times (V_{IN} - 1.4V)}{1.18 \times 10^{-10}} - 1.4\ k\Omega \quad (6)$$

To set a specific continuous conduction mode switching frequency (Fs), the R_{ON} resistor is determined from Equation 7.

$$R_{ON} = \frac{V_{OUT} \times (V_{IN} - 1.4V)}{V_{IN} \times F_S \times 1.18 \times 10^{-10}} - 1.4\ k\Omega \quad (7)$$

In high frequency applications the minimum value for t_{ON} is limited by the maximum duty cycle required for regulation and the minimum OFF-time of the LM25010 (260 ns, ±15%). The fixed OFF-time limits the maximum duty cycle achievable with a low voltage at VIN. The minimum allowed ON-time to regulate the desired V_{OUT} at the minimum V_{IN} is determined from Equation 8.

$$t_{ON(min)} = \frac{V_{OUT} \times 300\ ns}{(V_{IN(min)} - V_{OUT})} \quad (8)$$

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Feature Description (continued)

7.3.6 Current Limit

Current limit detection occurs during the OFF-time by monitoring the recirculating current through the internal current sense resistor (R_{SENSE}). The detection threshold is 1.25 A, ±0.25 A. Referring to the *Functional Block Diagram*, if the current into SGND during the OFF-time exceeds the threshold level the current limit comparator delays the start of the next ON-time period. The next ON-time starts when the current into SGND is below the threshold and the voltage at FB is below 2.5 V. Figure 9 illustrates the inductor current waveform during normal operation and during current limit. The output current I_O is the average of the inductor ripple current waveform. The Low Load Current waveform illustrates continuous conduction mode operation with peak and valley inductor currents below the current limit threshold. When the load current is increased (High Load Current), the ripple waveform maintains the same amplitude and frequency since the current falls below the current limit threshold at the valley of the ripple waveform. Note the average current in the High Load Current portion of Figure 9 is above the current limit threshold. Since the current reduces below the threshold in the normal OFF-time each cycle, the start of each ON-time is not delayed, and the circuit's output voltage is regulated at the correct value. When the load current is further increased such that the lower peak would be above the threshold, the OFF-time is lengthened to allow the current to decrease to the threshold before the next ON-time begins (Current Limited portion of Figure 9). Both V_{OUT} and the switching frequency are reduced as the circuit operates in a constant current mode. The load current (I_{OCL}) is equal to the current limit threshold plus half the ripple current (ΔI/2). The ripple amplitude (ΔI) is calculated from Equation 9.

$$\Delta I = \frac{(V_{IN} - V_{OUT}) \times t_{ON}}{L1} \tag{9}$$

The current limit threshold can be increased by connecting an external resistor (R_{CL}) between SGND and ISEN. R_{CL} typically is less than 1 Ω, and the calculation of its value is explained in *Application and Implementation*. If the current limit threshold is increased by adding R_{CL}, the maximum continuous load current should not exceed 1.5 A, and the peak current out of the SW pin should not exceed 2 A.

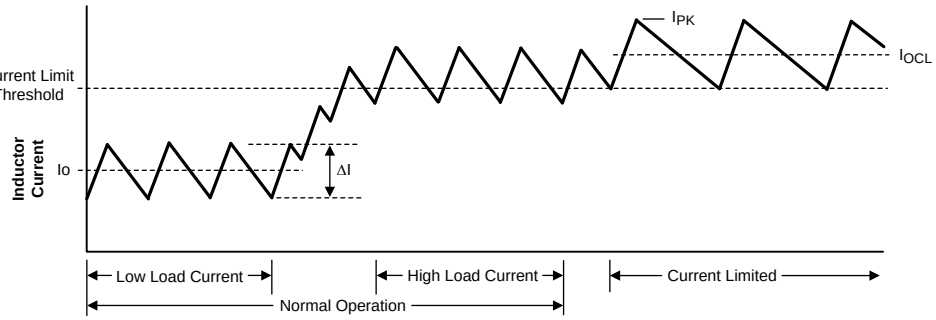

Figure 9. Inductor Current - Current Limit Operation

7.3.7 Soft Start

The soft-start feature allows the regulator to gradually reach a steady-state operating point, thereby reducing start-up stresses and current surges. At turnon, while V_{CC} is below the undervoltage threshold (t1 in Figure 1), the SS pin is internally grounded, and V_{OUT} is held at 0 V. When V_{CC} exceeds the undervoltage threshold (UVLO) an internal 11.5-µA current source charges the external capacitor (C6) at the SS pin to 2.5 V (t2 in Figure 1). The increasing SS voltage at the non-inverting input of the regulation comparator gradually increases the output voltage from zero to the desired value. The soft-start feature keeps the load inductor current from reaching the current limit threshold during start-up, thereby reducing inrush currents.

An internal switch grounds the SS pin if V_{CC} is below the undervoltage lockout threshold, or if the circuit is shutdown using the RON/SD pin.

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Feature Description (continued)

7.3.8 N-Channel Buck Switch and Driver

The LM25010 integrates an N-Channel buck switch and associated floating high voltage gate driver. The peak current through the buck switch should not exceed 2A, and the load current should not exceed 1.5A. The gate driver circuit is powered by the external bootstrap capacitor between BST and SW (C4), which is recharged each OFF-time from V_{CC} through the internal high voltage diode. The minimum OFF-time, nominally 260 ns, ensures sufficient time during each cycle to recharge the bootstrap capacitor. A 0.022 µF ceramic capacitor is recommended for C4.

7.3.9 Thermal Shutdown

The LM25010 should be operated below the maximum operating junction temperature rating. If the junction temperature increases during a fault or abnormal operating condition, the internal Thermal Shutdown circuit activates typically at 175°C. The Thermal Shutdown circuit reduces power dissipation by disabling the buck switch and the ON timer. This feature helps prevent catastrophic failures from accidental device overheating. When the junction temperature reduces below approximately 155°C (20°C typical hysteresis), normal operation resumes.

7.4 Device Functional Modes

7.4.1 Shutdown

The LM25010 can be remotely shut down by forcing the RON/SD pin below 0.7 V with a switch or open drain device. See Figure 10. In the shutdown mode the SS pin is internally grounded, the ON-time one-shot is disabled, the input current at VIN is reduced, and the V_{CC} bypass switch is turned off. The V_{CC} regulator is not disabled in the shutdown mode. Releasing the RON/SD pin allows normal operation to resume. The nominal voltage at RON/SD is shown in Figure 6. When switching the RON/SD pin, the transition time should be faster than one to two cycles of the regulator's nominal switching frequency.

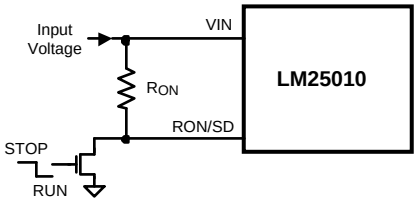

Figure 10. Shutdown Implementation

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8 Application and Implementation

NOTE

Information in the following applications sections is not part of the TI component specification, and TI does not warrant its accuracy or completeness. TI's customers are responsible for determining suitability of components for their purposes. Customers should validate and test their design implementation to confirm system functionality.

8.1 Application Information

The LM25010 is a non-synchronous buck regulator converter designed to operate over a wide input voltage and output current range. Spreadsheet-based calculator tools, available on the TI product website at Quick-Start Calculator, can be used to design a single output non-synchronous buck converter.

Alternatively, online WEBENCH® software is available to create a complete buck design and generate the bill of materials, estimated efficiency, solution size, and cost of the complete solution.

8.2 Typical Application

The final circuit is shown in Figure 11, and its performance is shown in Figure 16 and Figure 17. Current limit measured approximately 1.3 A.

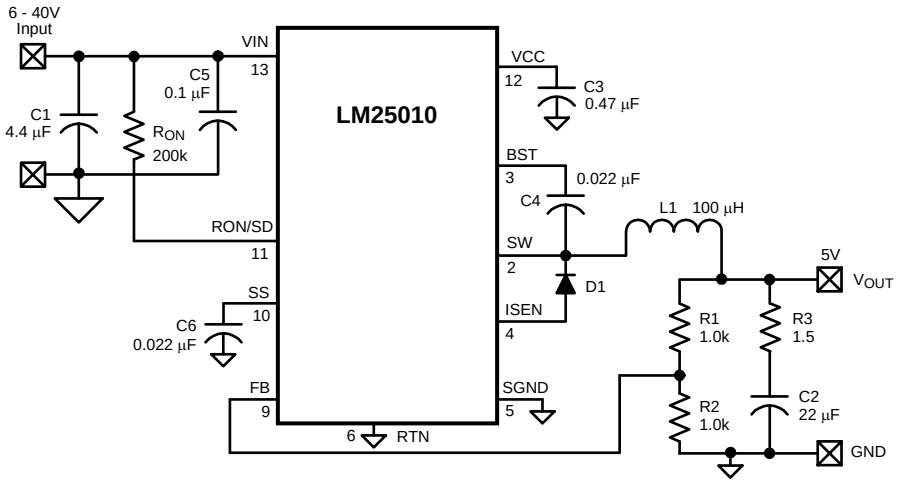

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Figure 11. LM25010 Example Circuit

8.2.1 Design Requirements

Table 1 lists the operating parameters for Figure 11.

Table 1. Design Parameters

PARAMETER	EXAMPLE VALUE
Input voltage	6 V to 40 V
Output voltage	5 V
Load current	200 mA to 1 A
Soft-start time	5 ms

8.2.2 Detailed Design Procedure

The procedure for calculating the external components is illustrated with a design example. Configure the circuit in Figure 11 according to the components listed in Table 2.

Table 2. List of Components for LM25010 Example Circuit

ITEM	DESCRIPTION	VALUE
C1	Ceramic capacitor	(2) 2.2 µF, 50 V
C2	Ceramic capacitor	22 µF, 16 V
C3	Ceramic capacitor	0.47 µF, 16 V
C4, C6	Ceramic capacitor	0.022 µF, 16 V
C5	Ceramic capacitor	0.1 µF, 50 V
D1	Schottky diode	60 V, 2 A
L1	Inductor	100 µH
R1	Resistor	1 kΩ
R2	Resistor	1 kΩ
R3	Resistor	1.5 Ω
R_{ON}	Resistor	200 kΩ
U1	LM25010	—

8.2.2.1 Component Selection

8.2.2.1.1 R1 and R2

These resistors set the output voltage, and calculate the ratio with Equation 10.

$$R1/R2 = (V_{OUT}/2.5V) - 1 \quad (10)$$

R1/R2 calculates to 1. The resistors should be chosen from standard value resistors in the range of 1 kΩ to 10 kΩ. A value of 1 kΩ is used for R1 and R2.

8.2.2.1.2 R_{ON}, F_S

R_{ON} can be chosen using Equation 7 to set the nominal frequency, or from Equation 6 if the ON-time at a particular V_{IN} is important. A higher frequency generally means a smaller inductor and capacitors (value, size and cost), but higher switching losses. A lower frequency means a higher efficiency, but with larger components. Generally, if PC board space is tight, a higher frequency is better. The resulting ON-time and frequency have a ±25% tolerance. Using Equation 7 at a nominal V_{IN} of 8 V in Equation 11.

$$R_{ON} = \frac{5V \times (8V - 1.4V)}{8V \times 175\ kHz \times 1.18 \times 10^{-10}} - 1.4\ k\Omega = 198\ k\Omega \quad (11)$$

A value of 200 kΩ will be used for R_{ON}, yielding a nominal frequency of 161 kHz at V_{IN} = 6 V, and 203 kHz at V_{IN} = 40 V.

8.2.2.1.3 L1

The inductor value is determined based on the load current, ripple current, and the minimum and maximum input voltage ($V_{IN(min)}$, $V_{IN(max)}$). See Figure 12.

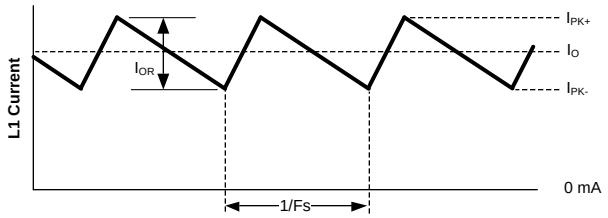

Figure 12. Inductor Current

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To keep the circuit in continuous conduction mode, the maximum allowed ripple current is twice the minimum load current, or 400 mA_{P-P}. Using this value of ripple current, the inductor (L1) is calculated using Equation 12 and Equation 13.

$$L1 = \frac{V_{OUT} \times (V_{IN(max)} - V_{OUT})}{I_{OR} \times F_{S(min)} \times V_{IN(max)}}$$

where

- $F_{S(min)}$ is the minimum frequency of 152 kHz (203 kHz – 25%) at $V_{IN(max)}$ (12)

$$L1 = \frac{5V \times (40V - 5V)}{0.40A \times 152\ kHz \times 40V} = 72\ \mu H \quad (13)$$

Equation 13 provides the minimum value for inductor L1. When selecting an inductor, use a higher standard value (100 uH). To prevent saturation, and possible destructive current levels, L1 must be rated for the peak current which occurs if the current limit and maximum ripple current are reached simultaneously (I_{PK} in Figure 9). The maximum ripple amplitude is calculated by rearranging Equation 12 using $V_{IN(max)}$, $F_{S(min)}$, and the minimum inductor value, based on the manufacturer's tolerance. Assume, for Equation 14, Equation 15, and Equation 16, the inductor's tolerance is ±20%.

$$I_{OR(max)} = \frac{V_{OUT} \times (V_{IN(max)} - V_{OUT})}{L1_{min} \times F_{S(min)} \times V_{IN(max)}} \quad (14)$$

$$I_{OR(max)} = \frac{5V \times (40V - 5V)}{80\ \mu H \times 152\ kHz \times 40V} = 360\ mAp\text{-}p \quad (15)$$

$$I_{PK} = I_{LIM} + I_{OR(max)} = 1.5\ A + 0.36\ A = 1.86\ A$$

where

- I_{LIM} is the maximum current limit threshold (16)

At the nominal maximum load current of 1 A, the peak inductor current is 1.18 A.

8.2.2.1.4 R_{CL}

Since it is obvious that the lower peak of the inductor current waveform does not exceed 1 A at maximum load current (see Figure 12), it is not necessary to increase the current limit threshold. Therefore R_{CL} is not needed for this exercise. For applications where the lower peak exceeds 1 A, see *Increasing The Current Limit Threshold*.

8.2.2.1.5 C2 and R3

Since the LM25010 requires a minimum of 25 mV_{P-P} of ripple at the FB pin for proper operation, the required ripple at V_{OUT} is increased by R1 and R2, and is equal to Equation 17.

$$V_{RIPPLE} = 25\ mV_{P-P} \times (R1 + R2) / R2 = 50\ mV_{P-P} \quad (17)$$

This necessary ripple voltage is created by the inductor ripple current acting on C2's ESR + R3. First, determine the minimum ripple current, which occurs at minimum V_{IN}, maximum inductor value, and maximum frequency with Equation 18.

$$I_{OR(min)} = \frac{V_{OUT} \times (V_{IN(min)} - V_{OUT})}{L1_{max} \times F_{S(max)} \times V_{IN(min)}}$$

$$= \frac{5V \times (6V - 5V)}{120\ \mu H \times 201\ kHz \times 6V} = 34.5\ mAp\text{-}p \quad (18)$$

The minimum ESR for C2 is then equal to Equation 19.

$$ESR_{(min)} = \frac{50\ mV}{34.5\ mA} = 1.45\Omega \quad (19)$$

If the capacitor used for C2 does not have sufficient ESR, R3 is added in series as shown in the *Functional Block Diagram*. The value chosen for C2 is application dependent, and it is recommended that it be no smaller than 3.3 µF. C2 affects the ripple at V_{OUT}, and transient response. Experimentation is usually necessary to determine the optimum value for C2.

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8.2.2.1.6 D1

A Schottky diode is recommended. Ultra-fast recovery diodes are not recommended as the high speed transitions at the SW pin may inadvertently affect the IC's operation through external or internal EMI. The diode should be rated for the maximum V_{IN} (40 V), the maximum load current (1 A), and the peak current which occurs when current limit and maximum ripple current are reached simultaneously (I_{PK} in Figure 9), previously calculated to be 1.86 A. The diode's forward voltage drop affects efficiency due to the power dissipated during the OFF-time. The average power dissipation in D1 is calculated from Equation 20.

$$P_{D1} = V_F \times I_O \times (1 - D) \quad (20)$$

where

- I_O is the load current
- D is the duty cycle

8.2.2.1.7 C1

This capacitor limits the ripple voltage at VIN resulting from the source impedance of the supply feeding this circuit, and the on/off nature of the switch current into VIN. At maximum load current, when the buck switch turns on, the current into VIN steps up from zero to the lower peak of the inductor current waveform (I_{PK-} in Figure 12), ramps up to the peak value (I_{PK+}), then drops to zero at turnoff. The average current into VIN during this ON-time is the load current. For a worst case calculation, C1 must supply this average current during the maximum ON-time. The maximum ON-time is calculated at V_{IN} = 6 V using Equation 5, with a 25% tolerance added to Equation 21.

$$t_{ON(max)} = \left[\frac{1.18 \times 10^{-10} \times (200k + 1.4k)}{6V - 1.4V} + 67\ ns\right] \times 1.25 = 6.5\ \mu s \quad (21)$$

The voltage at VIN should not be allowed to drop below 5.5 V in order to maintain V_{CC} above its UVLO in Equation 22.

$$C1 = \frac{I_O \times t_{ON}}{\Delta V} = \frac{1.0A \times 6.5\ \mu s}{0.5V} = 13\ \mu F \quad (22)$$

Normally a lower value can be used for C1 since the above calculation is a worst case calculation which assumes the power source has a high source impedance. A quality ceramic capacitor with a low ESR should be used for C1.

8.2.2.1.8 C3

The capacitor at the VCC pin provides noise filtering and stability, prevents false triggering of the V_{CC} UVLO at the buck switch ON and OFF transitions, and limits the peak voltage at V_{CC} when a high voltage with a short rise time is initially applied at V_{IN}. C3 should be no smaller than 0.47 µF, and must be a good quality, low ESR, ceramic capacitor, physically close to the IC pins.

8.2.2.1.9 C4

The recommended value for C4 is 0.022 µF. TI recommends a high quality ceramic capacitor with low ESR as C4 supplies the surge current to charge the buck switch gate at each turnon. A low ESR also ensures a complete recharge during each OFF-time.

8.2.2.1.10 C5

This capacitor suppresses transients and ringing due to lead inductance at VIN. TI recommends a low ESR, 0.1-µF ceramic chip capacitor placed physically close to the LM25010.

8.2.2.1.11 C6

The capacitor at the SS pin determines the softstart time (that is the time for the reference voltage at the regulation comparator and the output voltage) to reach their final value. Determine the capacitor value with Equation 23.

$$C6 = \frac{t_{SS} \times 11.5\ \mu A}{2.5V} \quad (23)$$

For a 5 ms softstart time, C6 calculates to 0.022 µF.

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8.2.2.2 Increasing The Current Limit Threshold

The current limit threshold is nominally 1.25 A, with a minimum guaranteed value of 1 A. If, at maximum load current, the lower peak of the inductor current (I_{PK-} in Figure 12) exceeds 1 A, resistor R_{CL} must be added between S_{GND} and I_{SEN} to increase the current limit threshold to be equal or exceed that lower peak current. This resistor diverts some of the recirculating current from the internal sense resistor so that a higher current level is needed to switch the internal current limit comparator. Calculate I_{PK-} with Equation 24.

$$I_{PK-} = I_{O(max)} - \frac{I_{OR(min)}}{2} \tag{24}$$

where

- $I_{O(max)}$ is the maximum load current
- $I_{OR(min)}$ is the minimum ripple current calculated using Equation 18

R_{CL} is calculated with Equation 25.

$$R_{CL} = \frac{1.0A \times 0.11\Omega}{I_{PK-} - 1.0A} \tag{25}$$

where

- 0.11 Ω is the minimum value of the internal resistance from S_{GND} to I_{SEN}

The next smaller standard value resistor should be used for R_{CL}. With the addition of R_{CL} it is necessary to check the average and peak current values to ensure they do not exceed the LM25010 limits. At maximum load current the average current through the internal sense resistor is calculated with Equation 26.

$$I_{AVE} = \frac{I_{O(max)} \times R_{CL} \times (V_{IN(max)} - V_{OUT})}{(R_{CL} + 0.11\Omega) \times V_{IN(max)}} \tag{26}$$

If I_{AVE} is less than 2 A, no changes are necessary. If it exceeds 2 A, R_{CL} must be reduced. The upper peak of the inductor current (I_{PK+}), at maximum load current, is calculated using Equation 27.

$$I_{PK+} = I_{O(max)} + \frac{I_{OR(max)}}{2} \tag{27}$$

where

- $I_{OR(max)}$ is calculated using Equation 14

If I_{PK+} exceeds 3.5 A , the inductor value must be increased to reduce the ripple amplitude. This necessitates recalculation of $I_{OR(min)}$, I_{PK-}, and R_{CL}.

When the circuit is in current limit, the upper peak current out of the SW pin is calculated with Equation 28.

$$I_{PK+(CL)} = \frac{1.5A \times (150\ m\Omega + R_{CL})}{R_{CL}} + I_{OR(MAX)} \tag{28}$$

The inductor L1 and diode D1 must be rated for this current.

8.2.2.3 Ripple Configurations

For applications where low output voltage ripple is required the output can be taken directly from the low ESR output capacitor (C2) as shown in Figure 13. However, R3 slightly degrades the load regulation. The specific component values, and the application determine if this is suitable.

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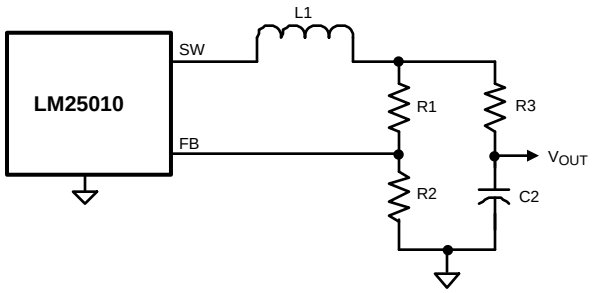

Figure 13. Low Ripple Output

Where the circuit of Figure 13 is not suitable, the circuits of Figure 14 or Figure 15 can be used.

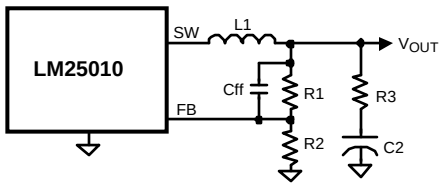

Figure 14. Low Output Ripple Using a Feedforward Capacitor

In Figure 14, Cff is added across R1 to AC-couple the ripple at V_{OUT} directly to the FB pin. This allows the ripple at V_{OUT} to be reduced, in some cases considerably, by reducing R3. In the circuit of Figure 11, the ripple at V_{OUT} ranged from 50 mV_{P-P} at V_{IN} = 6 V to 285 mV_{P-P} at V_{IN} = 40 V. By adding a 1000 pF capacitor at Cff and reducing R3 to 0.75 Ω, the V_{OUT} ripple was reduced by 50%, ranging from 25 mV_{P-P} to 142 mV_{P-P}.

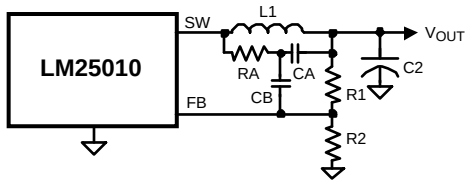

Figure 15. Low Output Ripple Using Ripple Injection

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To reduce V_{OUT} ripple further, the circuit of Figure 15 can be used. R3 has been removed, and the output ripple amplitude is determined by C2's ESR and the inductor ripple current. RA and CA are chosen to generate a 40 mV to 50 mV_{P-P} sawtooth at their junction, and that voltage is AC-coupled to the FB pin via CB. In selecting RA and CA, V_{OUT} is considered a virtual ground as the SW pin switches between V_{IN} and –1 V. Since the ON-time at SW varies inversely with V_{IN}, the waveform amplitude at the RA and CA junction is relatively constant. R1 and R2 must typically be increased to more than 5 kΩ each to not significantly attenuate the signal provided to FB through CB. Typical values for the additional components are RA = 200 kΩ, CA = 680 pF, and CB = 0.01 µF.

8.2.3 Application Curves

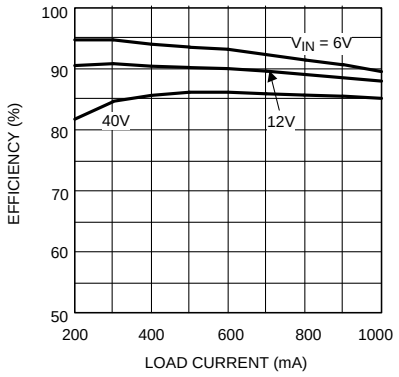

Figure 16. Efficiency vs Load Current and V_{IN} Circuit of Figure 11

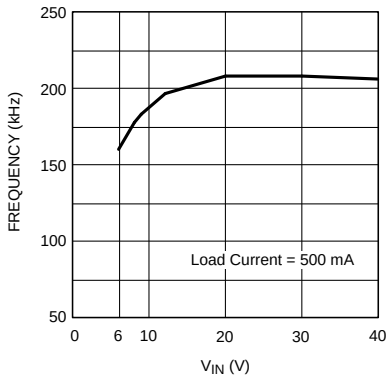

Figure 17. Frequency vs V_{IN} Circuit of Figure 11

8.3 Do's and Don'ts

A minimum load current of 1 mA is required to maintain proper operation. If the load current falls below that level, the bootstrap capacitor can discharge during the long OFF-time and the circuit either shuts down or cycles ON and OFF at a low frequency. If the load current is expected to drop below 1 mA in the application, choose the feedback resistors to be low enough in value to provide the minimum required current at nominal V_{OUT}.

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9 Power Supply Recommendations

The LM25010 is designed to operate with an input power supply capable of supplying a voltage range from 6 V to 42 V. The input power supply must be well-regulated and capable of supplying sufficient current to the regulator during peak load operation. Also, like in all applications, the power-supply source impedance must be small compared to the module input impedance to maintain the stability of the converter.

10 Layout

10.1 Layout Guidelines

The LM25010 regulation, overvoltage, and current limit comparators are very fast, and respond to short duration noise pulses. Therefore, layout considerations are critical for optimum performance. The layout must be as neat and compact as possible, and all the components must be as close as possible to their associated pins. The two major current loops have currents which switch very fast, and so the loops should be as small as possible to minimize conducted and radiated EMI. The first loop is that formed by C1 (C_{IN}), through the VIN to SW pins, L1 (L_{IND}), C2 (C_{OUT}), and back to C1. The second loop is that formed by D1, L1, C2, and the SGND and ISEN pins. The ground connection from C2 to C1 should be as short and direct as possible, preferably without going through vias. Directly connect the SGND and RTN pin to each other, and they should be connected as directly as possible to the C1/C2 ground line without going through vias. The power dissipation within the IC can be approximated by determining the total conversion loss ($P_{IN} – P_{OUT}$), and then subtracting the power losses in the free-wheeling diode and the inductor. The power loss in the diode is approximately Equation 29.

$$P_{D1} = I_O \times V_F \times (1 – D) \quad (29)$$

where I_O is the load current, V_F is the diode's forward voltage drop, and D is the duty cycle. The power loss in the inductor is approximately Equation 30.

$$P_{L1} = I_O^2 \times R_L \times 1.1$$

where

- R_L is the inductor's DC resistance
- the 1.1 factor is an approximation for the AC losses (30)

If it is expected that the internal dissipation of the LM25010 will produce high junction temperatures during normal operation, good use of the PC board's ground plane can help considerably to dissipate heat. The exposed pad on the IC package bottom should be soldered to a ground plane, and that plane should both extend from beneath the IC, and be connected to exposed ground plane on the board's other side using as many vias as possible. The exposed pad is internally connected to the IC substrate. The use of wide PC board traces at the pins, where possible, can help conduct heat away from the IC. The four NC pins on the HTSSOP package are not electrically connected to any part of the IC, and may be connected to ground plane to help dissipate heat from the package. Judicious positioning of the PC board within the end product, along with the use of any available air flow (forced or natural convection) can help reduce the junction temperature.

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10.2 Layout Example

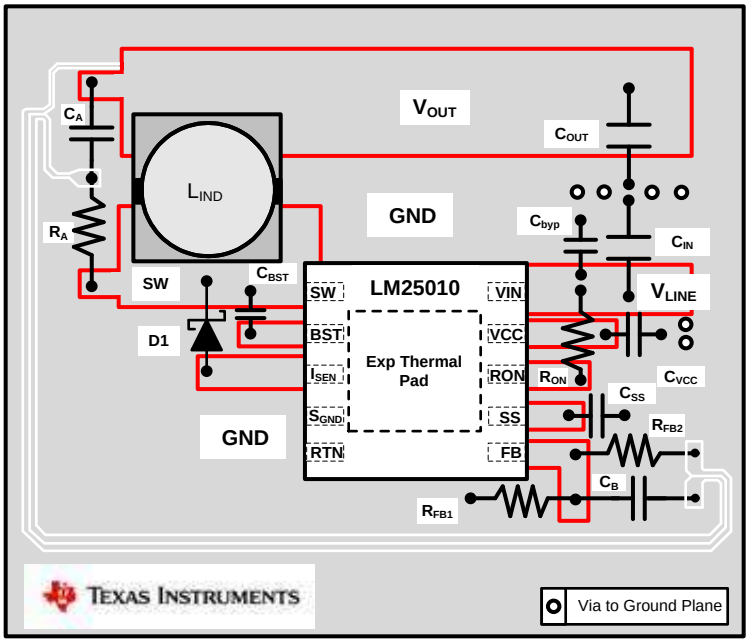

Figure 18. LM25010 Buck Layout Example With the WSON Package

11 Device and Documentation Support

11.1 Related Links

The table below lists quick access links. Categories include technical documents, support and community resources, tools and software, and quick access to sample or buy.

Table 3. Related Links

PARTS	PRODUCT FOLDER	SAMPLE & BUY	TECHNICAL DOCUMENTS	TOOLS & SOFTWARE	SUPPORT & COMMUNITY
LM25010	Click here	Click here	Click here	Click here	Click here
LM25010-Q1	Click here	Click here	Click here	Click here	Click here

11.2 Community Resources

The following links connect to TI community resources. Linked contents are provided "AS IS" by the respective contributors. They do not constitute TI specifications and do not necessarily reflect TI's views; see TI's Terms of Use.

TI E2E™ Online Community ***TI's Engineer-to-Engineer (E2E) Community.*** Created to foster collaboration among engineers. At e2e.ti.com, you can ask questions, share knowledge, explore ideas and help solve problems with fellow engineers.

Design Support ***TI's Design Support*** Quickly find helpful E2E forums along with design support tools and contact information for technical support.

11.3 Trademarks

E2E is a trademark of Texas Instruments.
All other trademarks are the property of their respective owners.

11.4 Electrostatic Discharge Caution

These devices have limited built-in ESD protection. The leads should be shorted together or the device placed in conductive foam during storage or handling to prevent electrostatic damage to the MOS gates.

11.5 Glossary

SLYZ022 — *TI Glossary*.

This glossary lists and explains terms, acronyms, and definitions.

12 Mechanical, Packaging, and Orderable Information

The following pages include mechanical, packaging, and orderable information. This information is the most current data available for the designated devices. This data is subject to change without notice and revision of this document. For browser-based versions of this data sheet, refer to the left-hand navigation.

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PACKAGING INFORMATION

Orderable part number	Status (1)	Material type (2)	Package | Pins	Package qty | Carrier	RoHS (3)	Lead finish/ Ball material (4)	MSL rating/ Peak reflow (5)	Op temp (°C)	Part marking (6)
LM25010MH/NOPB	Active	Production	HTSSOP (PWP) | 14	94 | TUBE	Yes	SN	Level-1-260C-UNLIM	-40 to 125	L25010 MH
LM25010MH/NOPB.A	Active	Production	HTSSOP (PWP) | 14	94 | TUBE	Yes	SN	Level-1-260C-UNLIM	-40 to 125	L25010 MH
LM25010MH/NOPB.B	Active	Production	HTSSOP (PWP) | 14	94 | TUBE	Yes	SN	Level-1-260C-UNLIM	-40 to 125	L25010 MH
LM25010MHX/NOPB	Active	Production	HTSSOP (PWP) | 14	2500 | LARGE T&R	Yes	SN	Level-1-260C-UNLIM	-40 to 125	L25010 MH
LM25010MHX/NOPB.A	Active	Production	HTSSOP (PWP) | 14	2500 | LARGE T&R	Yes	SN	Level-1-260C-UNLIM	-40 to 125	L25010 MH
LM25010MHX/NOPB.B	Active	Production	HTSSOP (PWP) | 14	2500 | LARGE T&R	Yes	SN	Level-1-260C-UNLIM	-40 to 125	L25010 MH
LM25010Q0MH/NOPB	Active	Production	HTSSOP (PWP) | 14	94 | TUBE	Yes	SN	Level-1-260C-UNLIM	-40 to 150	L25010 Q0MH
LM25010Q0MH/NOPB.A	Active	Production	HTSSOP (PWP) | 14	94 | TUBE	Yes	SN	Level-1-260C-UNLIM	-40 to 150	L25010 Q0MH
LM25010Q0MH/NOPB.B	Active	Production	HTSSOP (PWP) | 14	94 | TUBE	Yes	SN	Level-1-260C-UNLIM	-40 to 150	L25010 Q0MH
LM25010Q0MHX/NOPB	Active	Production	HTSSOP (PWP) | 14	2500 | LARGE T&R	Yes	SN	Level-1-260C-UNLIM	-40 to 150	L25010 Q0MH
LM25010Q0MHX/NOPB.A	Active	Production	HTSSOP (PWP) | 14	2500 | LARGE T&R	Yes	SN	Level-1-260C-UNLIM	-40 to 150	L25010 Q0MH
LM25010Q0MHX/NOPB.B	Active	Production	HTSSOP (PWP) | 14	2500 | LARGE T&R	Yes	SN	Level-1-260C-UNLIM	-40 to 150	L25010 Q0MH
LM25010Q1MH/NOPB	Active	Production	HTSSOP (PWP) | 14	94 | TUBE	Yes	SN	Level-1-260C-UNLIM	-40 to 125	L25010 Q1MH
LM25010Q1MH/NOPB.A	Active	Production	HTSSOP (PWP) | 14	94 | TUBE	Yes	SN	Level-1-260C-UNLIM	-40 to 150	L25010 Q1MH
LM25010Q1MH/NOPB.B	Active	Production	HTSSOP (PWP) | 14	94 | TUBE	Yes	SN	Level-1-260C-UNLIM	-40 to 150	L25010 Q1MH
LM25010Q1MHX/NOPB	Active	Production	HTSSOP (PWP) | 14	2500 | LARGE T&R	Yes	SN	Level-1-260C-UNLIM	-40 to 125	L25010 Q1MH

Orderable part number	Status (1)	Material type (2)	Package | Pins	Package qty | Carrier	RoHS (3)	Lead finish/ Ball material (4)	MSL rating/ Peak reflow (5)	Op temp (°C)	Part marking (6)
LM25010Q1MHX/NOPB.A	Active	Production	HTSSOP (PWP) | 14	2500 | LARGE T&R	Yes	SN	Level-1-260C-UNLIM	-40 to 150	L25010 Q1MH
LM25010Q1MHX/NOPB.B	Active	Production	HTSSOP (PWP) | 14	2500 | LARGE T&R	Yes	SN	Level-1-260C-UNLIM	-40 to 150	L25010 Q1MH
LM25010SD/NOPB	Active	Production	WSON (DPR) | 10	1000 | SMALL T&R	Yes	NIPDAU | SN	Level-1-260C-UNLIM	-40 to 125	25010SD
LM25010SD/NOPB.A	Active	Production	WSON (DPR) | 10	1000 | SMALL T&R	Yes	SN	Level-1-260C-UNLIM	-40 to 125	25010SD
LM25010SD/NOPB.B	Active	Production	WSON (DPR) | 10	1000 | SMALL T&R	Yes	SN	Level-1-260C-UNLIM	-40 to 125	25010SD
LM25010SDX/NOPB	Active	Production	WSON (DPR) | 10	4500 | LARGE T&R	Yes	NIPDAU | SN	Level-1-260C-UNLIM	-40 to 125	25010SD
LM25010SDX/NOPB.A	Active	Production	WSON (DPR) | 10	4500 | LARGE T&R	Yes	SN	Level-1-260C-UNLIM	-40 to 125	25010SD
LM25010SDX/NOPB.B	Active	Production	WSON (DPR) | 10	4500 | LARGE T&R	Yes	SN	Level-1-260C-UNLIM	-40 to 125	25010SD

(1) **Status:** For more details on status, see our product life cycle.

(2) **Material type:** When designated, preproduction parts are prototypes/experimental devices, and are not yet approved or released for full production. Testing and final process, including without limitation quality assurance, reliability performance testing, and/or process qualification, may not yet be complete, and this item is subject to further changes or possible discontinuation. If available for ordering, purchases will be subject to an additional waiver at checkout, and are intended for early internal evaluation purposes only. These items are sold without warranties of any kind.

(3) **RoHS values:** Yes, No, RoHS Exempt. See the TI RoHS Statement for additional information and value definition.

(4) **Lead finish/Ball material:** Parts may have multiple material finish options. Finish options are separated by a vertical ruled line. Lead finish/Ball material values may wrap to two lines if the finish value exceeds the maximum column width.

(5) **MSL rating/Peak reflow:** The moisture sensitivity level ratings and peak solder (reflow) temperatures. In the event that a part has multiple moisture sensitivity ratings, only the lowest level per JEDEC standards is shown. Refer to the shipping label for the actual reflow temperature that will be used to mount the part to the printed circuit board.

(6) **Part marking:** There may be an additional marking, which relates to the logo, the lot trace code information, or the environmental category of the part.

Multiple part markings will be inside parentheses. Only one part marking contained in parentheses and separated by a "~" will appear on a part. If a line is indented then it is a continuation of the previous line and the two combined represent the entire part marking for that device.

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OTHER QUALIFIED VERSIONS OF LM25010, LM25010-Q1 :

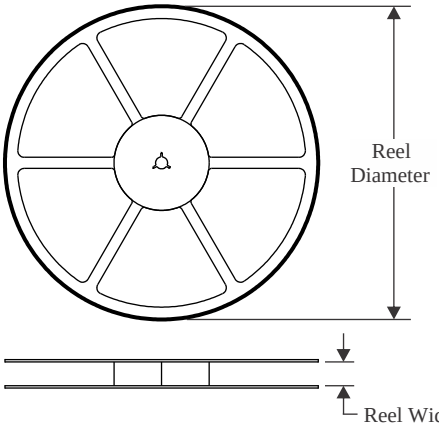
- Catalog : LM25010
- Automotive : LM25010-Q1

NOTE: Qualified Version Definitions:

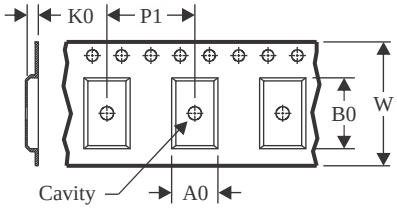
- Catalog - TI's standard catalog product
- Automotive - Q100 devices qualified for high-reliability automotive applications targeting zero defects

TAPE AND REEL INFORMATION

REEL DIMENSIONS

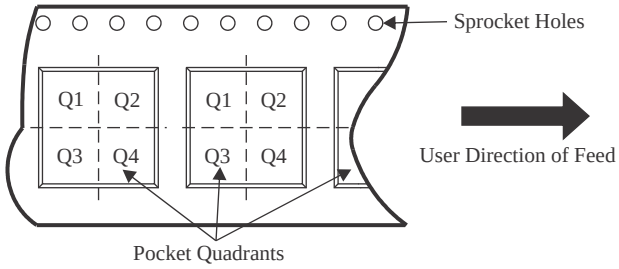


TAPE DIMENSIONS



A0	Dimension designed to accommodate the component width
B0	Dimension designed to accommodate the component length
K0	Dimension designed to accommodate the component thickness
W	Overall width of the carrier tape
P1	Pitch between successive cavity centers

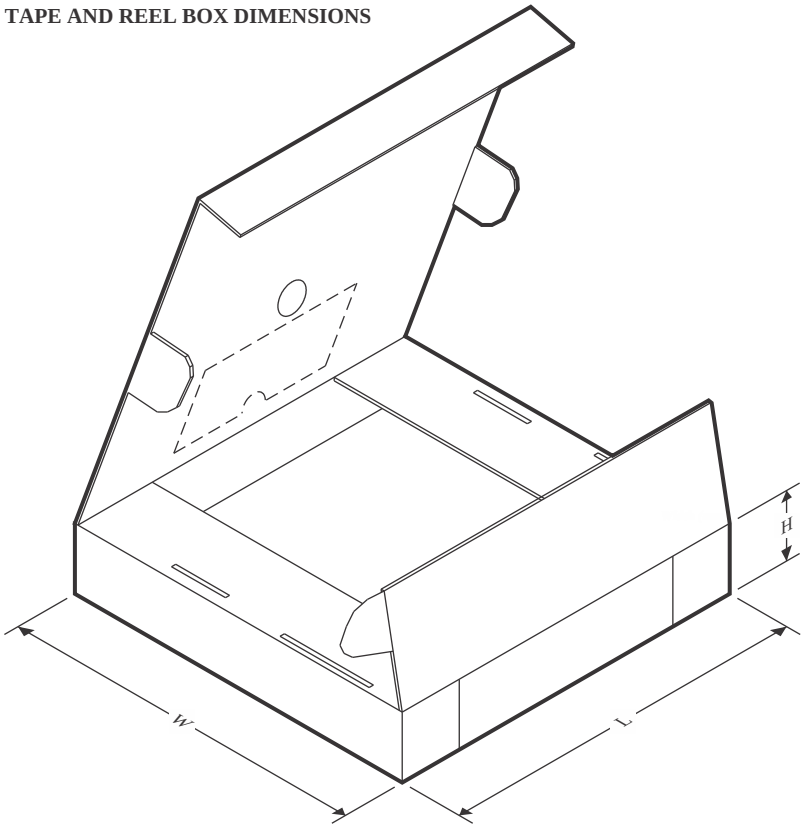
QUADRANT ASSIGNMENTS FOR PIN 1 ORIENTATION IN TAPE



*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Reel Diameter (mm)	Reel Width W1 (mm)	A0 (mm)	B0 (mm)	K0 (mm)	P1 (mm)	W (mm)	Pin1 Quadrant
LM25010MHX/NOPB	HTSSOP	PWP	14	2500	330.0	12.4	6.9	5.6	1.6	8.0	12.0	Q1
LM25010Q0MHX/NOPB	HTSSOP	PWP	14	2500	330.0	12.4	6.9	5.6	1.6	8.0	12.0	Q1
LM25010Q1MHX/NOPB	HTSSOP	PWP	14	2500	330.0	12.4	6.9	5.6	1.6	8.0	12.0	Q1
LM25010SD/NOPB	WSON	DPR	10	1000	177.8	12.4	4.3	4.3	1.3	8.0	12.0	Q1
LM25010SD/NOPB	WSON	DPR	10	1000	180.0	12.4	4.3	4.3	1.1	8.0	12.0	Q1
LM25010SDX/NOPB	WSON	DPR	10	4500	330.0	12.4	4.3	4.3	1.3	8.0	12.0	Q1
LM25010SDX/NOPB	WSON	DPR	10	4500	330.0	12.4	4.3	4.3	1.1	8.0	12.0	Q1

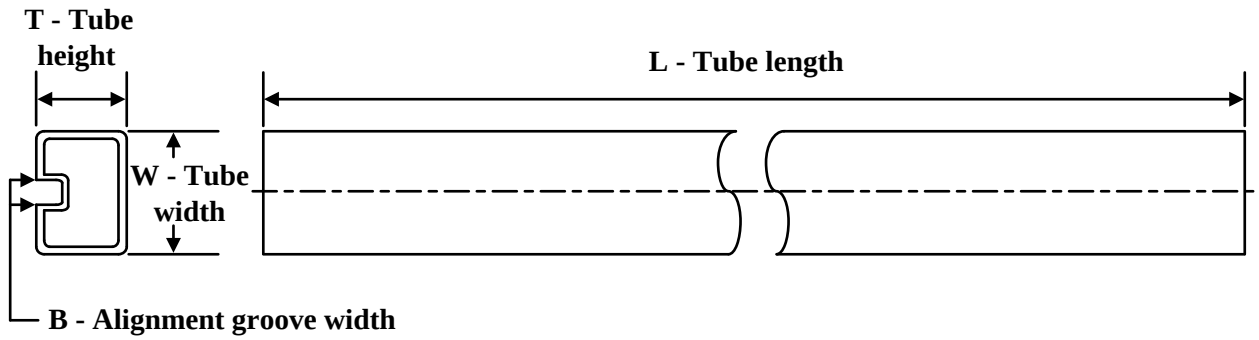
TAPE AND REEL BOX DIMENSIONS



*All dimensions are nominal

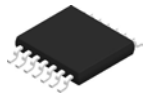
Device	Package Type	Package Drawing	Pins	SPQ	Length (mm)	Width (mm)	Height (mm)
LM25010MHX/NOPB	HTSSOP	PWP	14	2500	367.0	367.0	35.0
LM25010Q0MHX/NOPB	HTSSOP	PWP	14	2500	367.0	367.0	35.0
LM25010Q1MHX/NOPB	HTSSOP	PWP	14	2500	367.0	367.0	35.0
LM25010SD/NOPB	WSON	DPR	10	1000	210.0	185.0	35.0
LM25010SD/NOPB	WSON	DPR	10	1000	200.0	183.0	25.0
LM25010SDX/NOPB	WSON	DPR	10	4500	367.0	367.0	35.0
LM25010SDX/NOPB	WSON	DPR	10	4500	346.0	346.0	35.0

TUBE



*All dimensions are nominal

Device	Package Name	Package Type	Pins	SPQ	L (mm)	W (mm)	T (µm)	B (mm)
LM25010MH/NOPB	PWP	HTSSOP	14	94	495	8	2514.6	4.06
LM25010MH/NOPB.A	PWP	HTSSOP	14	94	495	8	2514.6	4.06
LM25010MH/NOPB.B	PWP	HTSSOP	14	94	495	8	2514.6	4.06
LM25010Q0MH/NOPB	PWP	HTSSOP	14	94	495	8	2514.6	4.06
LM25010Q0MH/NOPB.A	PWP	HTSSOP	14	94	495	8	2514.6	4.06
LM25010Q0MH/NOPB.B	PWP	HTSSOP	14	94	495	8	2514.6	4.06
LM25010Q1MH/NOPB	PWP	HTSSOP	14	94	495	8	2514.6	4.06
LM25010Q1MH/NOPB.A	PWP	HTSSOP	14	94	495	8	2514.6	4.06
LM25010Q1MH/NOPB.B	PWP	HTSSOP	14	94	495	8	2514.6	4.06

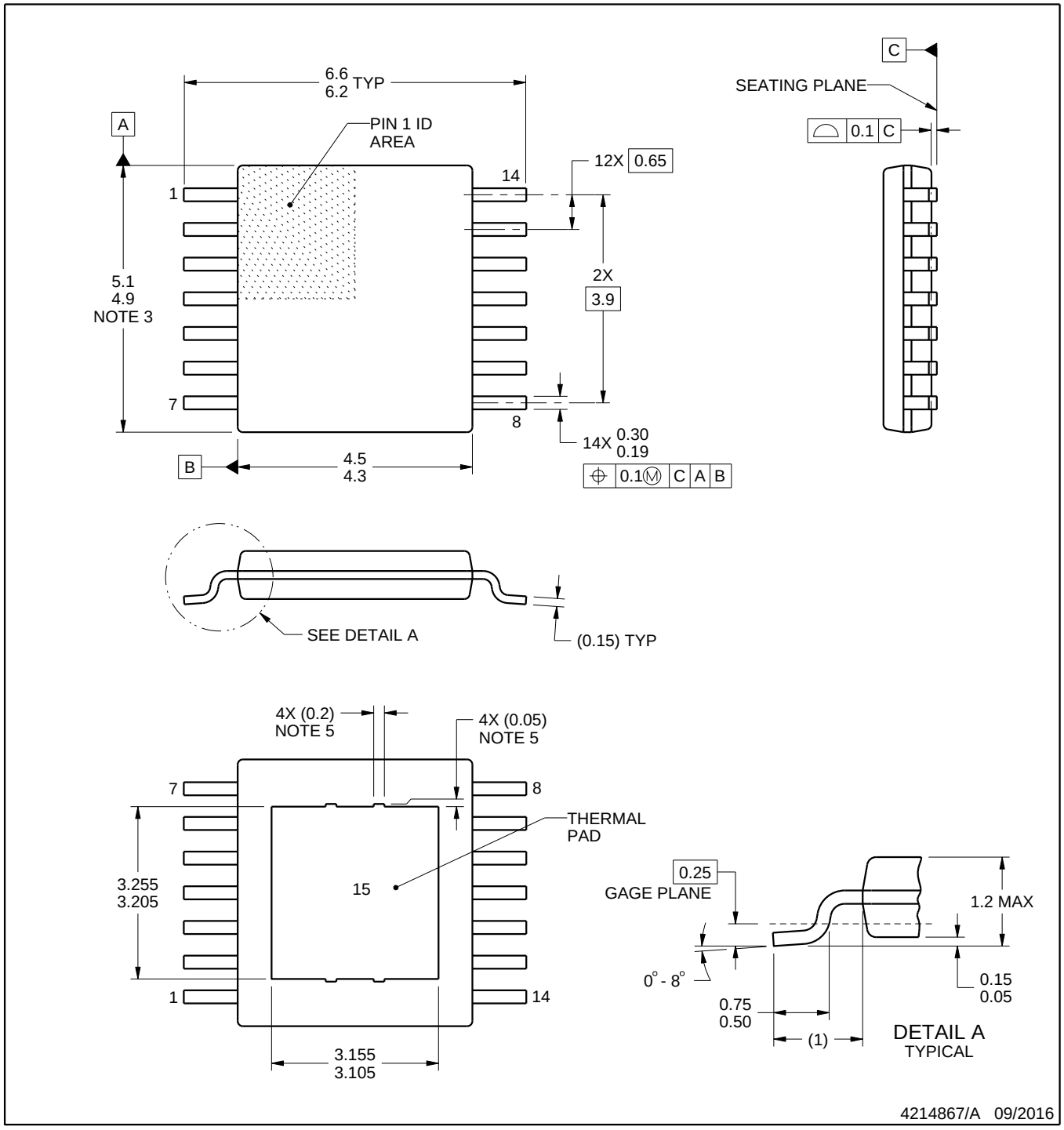


PACKAGE OUTLINE

PWP0014A

PowerPAD™ TSSOP - 1.2 mm max height

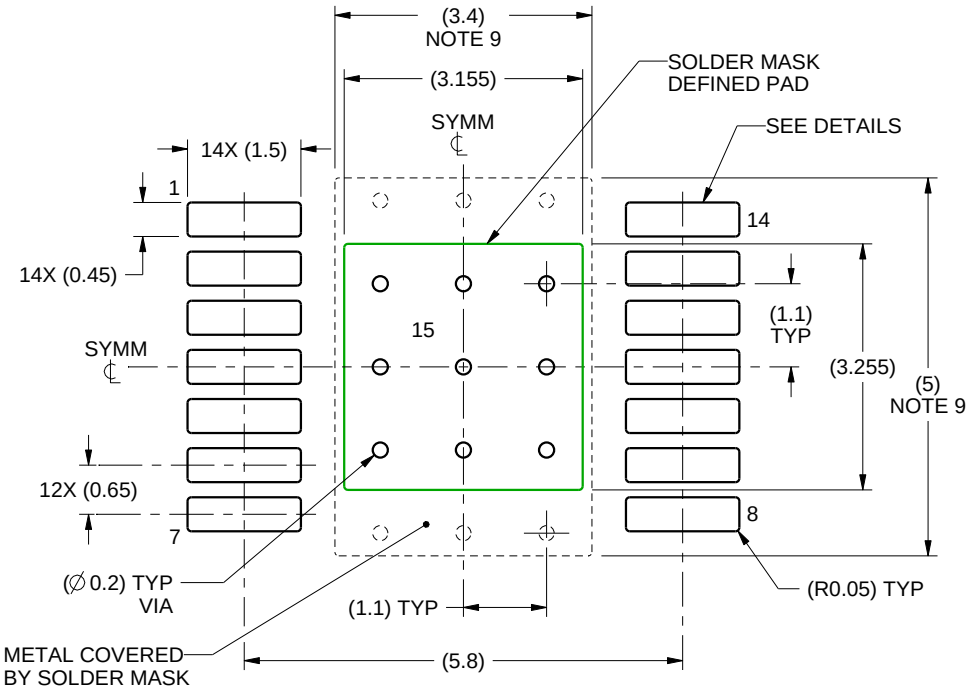
PLASTIC SMALL OUTLINE



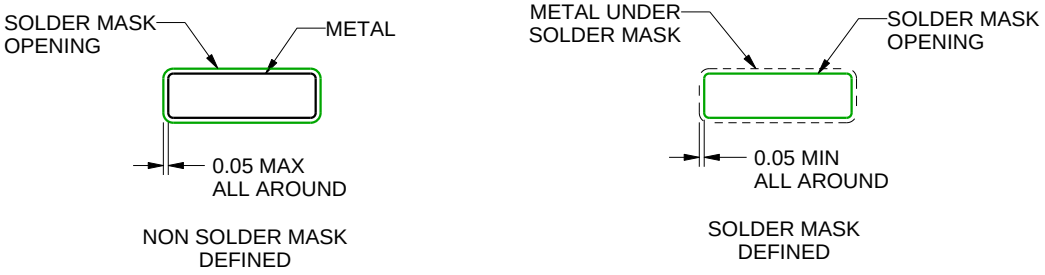
PowerPAD is a trademark of Texas Instruments.

NOTES:

1. All linear dimensions are in millimeters. Any dimensions in parenthesis are for reference only. Dimensioning and tolerancing per ASME Y14.5M.
2. This drawing is subject to change without notice.
3. This dimension does not include mold flash, protrusions, or gate burrs. Mold flash, protrusions, or gate burrs shall not exceed 0.15 mm per side.
4. Reference JEDEC registration MO-153.
5. Features may differ and may not be present.



LAND PATTERN EXAMPLE
SCALE:10X

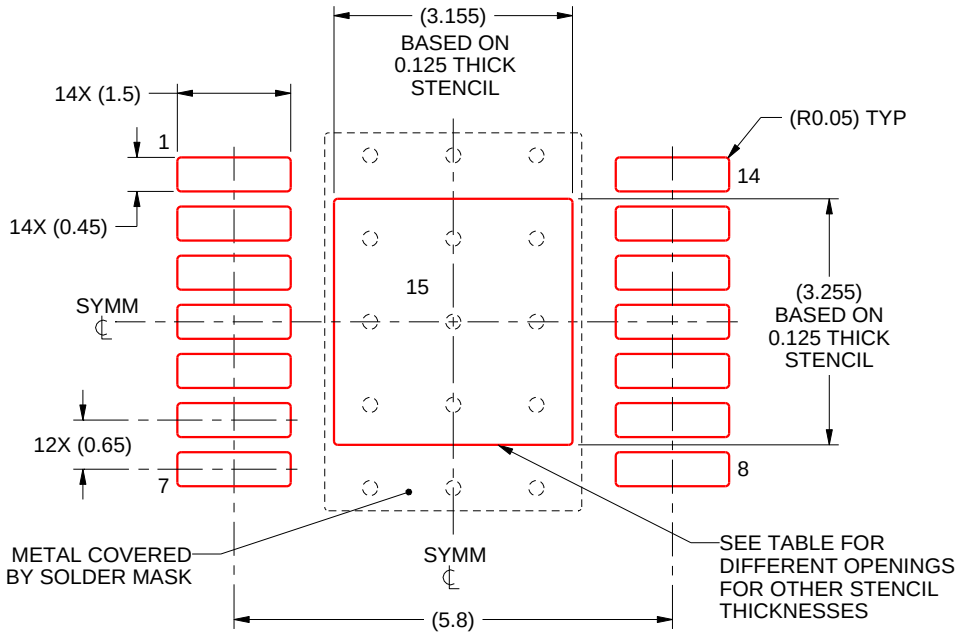


SOLDER MASK DETAILS
PADS 1-14

4214867/A 09/2016

NOTES: (continued)

6. Publication IPC-7351 may have alternate designs.
7. Solder mask tolerances between and around signal pads can vary based on board fabrication site.
8. This package is designed to be soldered to a thermal pad on the board. For more information, see Texas Instruments literature numbers SLMA002 (www.ti.com/lit/slma002) and SLMA004 (www.ti.com/lit/slma004).
9. Size of metal pad may vary due to creepage requirement.



SOLDER PASTE EXAMPLE
EXPOSED PAD
100% PRINTED SOLDER COVERAGE BY AREA
SCALE:10X

STENCIL THICKNESS	SOLDER STENCIL OPENING
0.1	3.53 X 3.64
0.125	3.155 X 3.255 (SHOWN)
0.15	2.88 X 2.97
0.175	2.67 X 2.75

4214867/A 09/2016

NOTES: (continued)

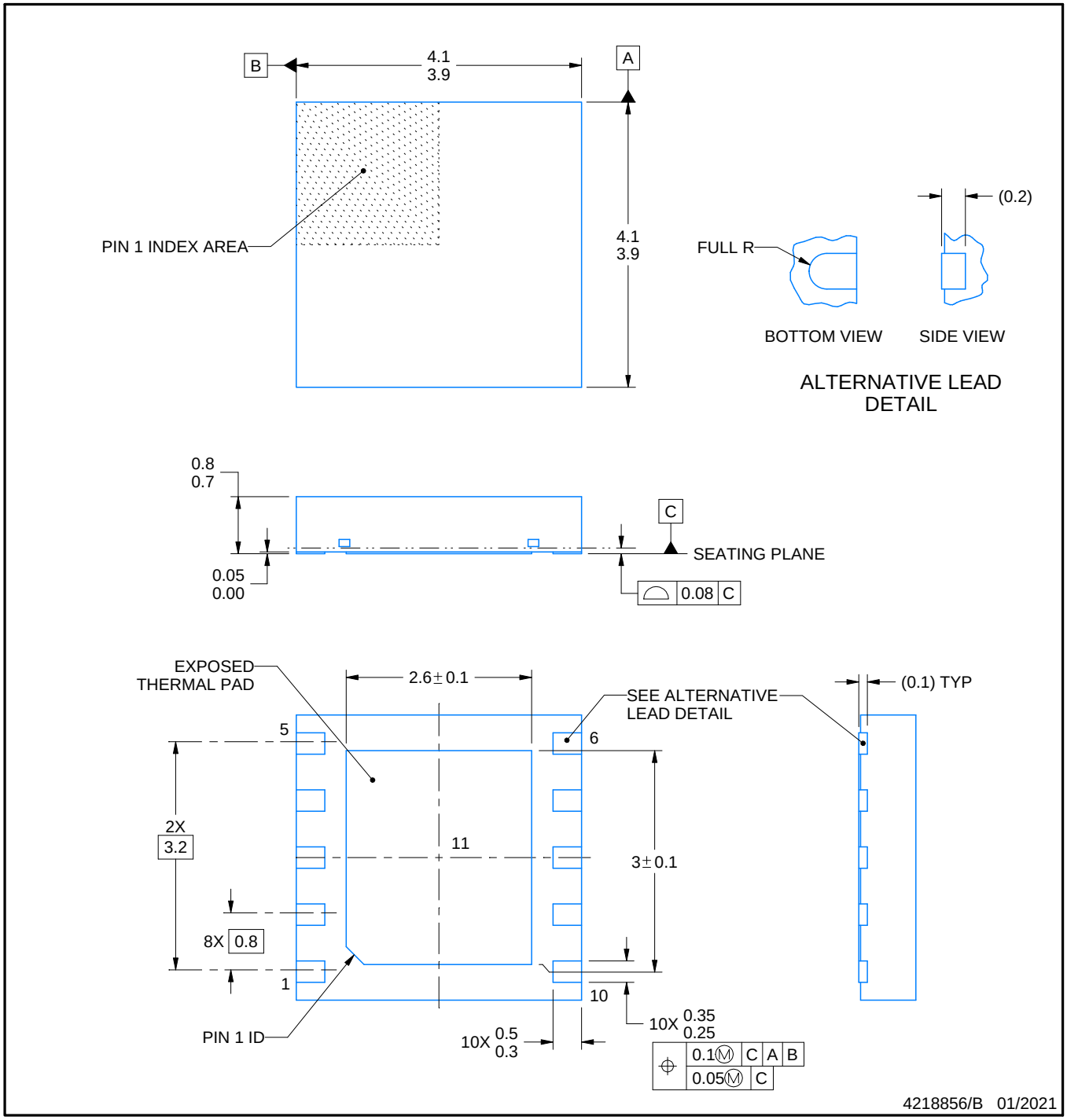
10. Laser cutting apertures with trapezoidal walls and rounded corners may offer better paste release. IPC-7525 may have alternate design recommendations.
11. Board assembly site may have different recommendations for stencil design.

PACKAGE OUTLINE

DPR0010A

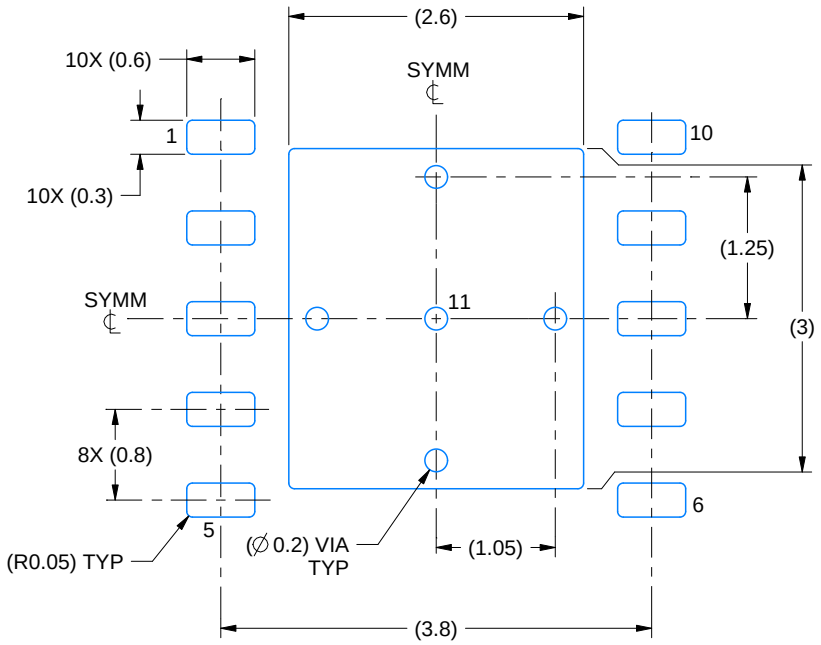
WSON - 0.8 mm max height

PLASTIC SMALL OUTLINE - NO LEAD

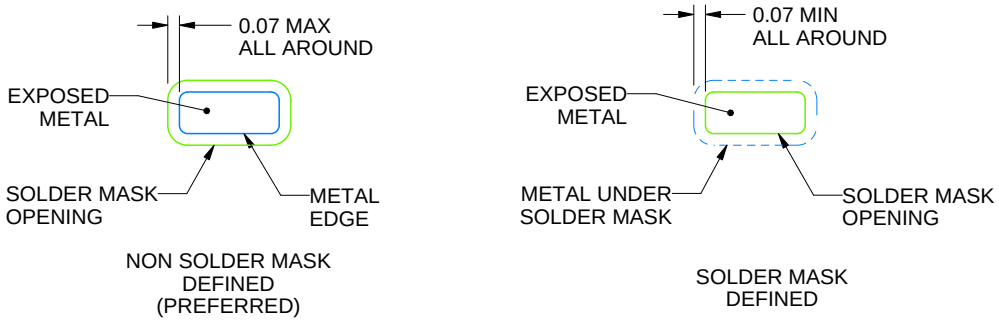


NOTES:

1. All linear dimensions are in millimeters. Any dimensions in parenthesis are for reference only. Dimensioning and tolerancing per ASME Y14.5M.
2. This drawing is subject to change without notice.
3. The package thermal pad must be soldered to the printed circuit board for thermal and mechanical performance.



LAND PATTERN EXAMPLE
EXPOSED METAL SHOWN
SCALE:15X

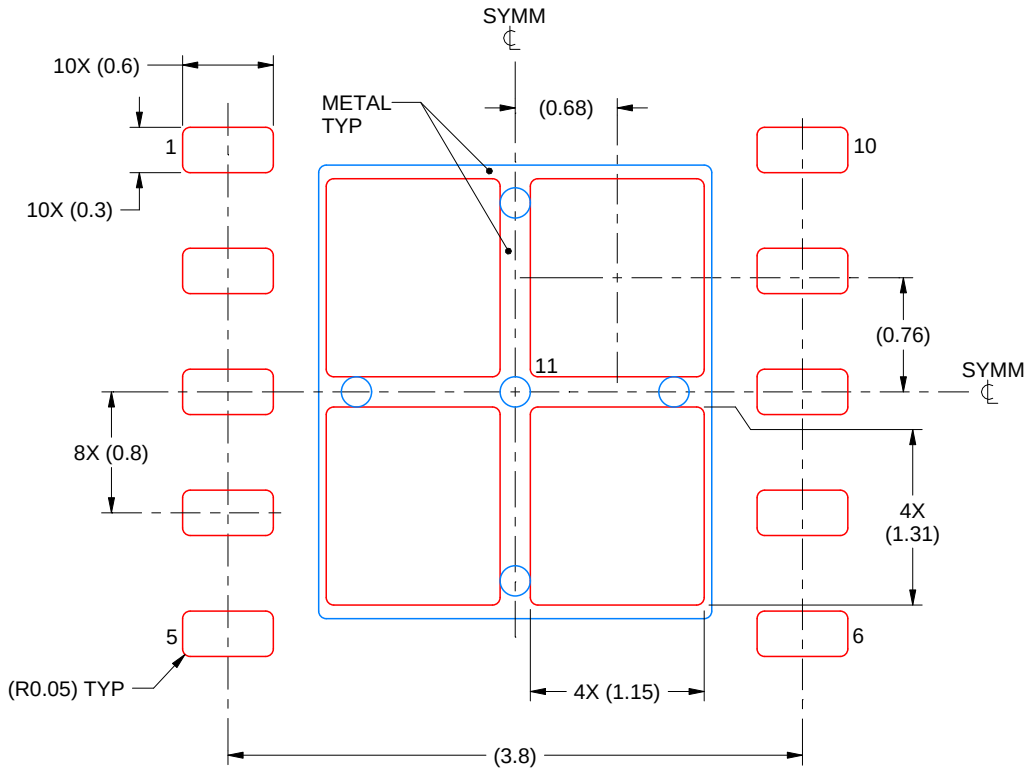


SOLDER MASK DETAILS

4218856/B 01/2021

NOTES: (continued)

4. This package is designed to be soldered to a thermal pad on the board. For more information, see Texas Instruments literature number SLUA271 (www.ti.com/lit/slua271).



SOLDER PASTE EXAMPLE
BASED ON 0.125 mm THICK STENCIL

EXPOSED PAD 11:
77% PRINTED SOLDER COVERAGE BY AREA
SCALE:20X

4218856/B 01/2021

NOTES: (continued)

5. Laser cutting apertures with trapezoidal walls and rounded corners may offer better paste release. IPC-7525 may have alternate design recommendations.

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