

TPS2HC120-Q1 120mΩ, 2A, Dual-Channel Automotive Smart High-Side Switch

1 Features

- Dual-channel 120mΩ automotive smart high-side switch with full diagnostics
 - Open-drain status output
 - Current sense analog output
- Wide operating voltage 3V to 28V
- Low power mode (LPM) with automatic entry and exit
 - $I_{Q,LPM} < 20\mu A/ch$ with both channels ON
- Ultra-low sleep current, $< 1\mu A$ at 25°C
- Selectable current limit, 0.25A to 4.7A
- Protection
 - Overload and short-circuit protection
 - Thermal shutdown and swing with self recovery
 - Inductive load negative voltage clamp
 - Loss-of-GND, loss-of-battery, and reverse battery protection
- Diagnostics
 - Fault report for fast interrupt
 - Overcurrent and short-to-ground detection
 - Open-load and short-to-battery detection
- Qualified for automotive applications
 - AEC-Q100 qualified with the following results:
 - Device temperature grade 1: $-40^{\circ}C$ to $125^{\circ}C$ ambient operating temperature range
 - Electrical transient disturbance immunity certification of ISO7637-2 and ISO16750-2
- 28-pin thermally-enhanced HVSSOP package
- **Functional Safety Capable**
 - [Documentation available to aid functional safety system design](#)

2 Applications

- [Body control module](#)
- [ADAS modules](#)
- [Automotive display module](#)

3 Description

TPS2HC120-Q1 is an automotive dual-channel, smart high-side switch, with integrated NMOS power FET and charge pump, designed to meet the requirements of 12V automotive battery systems. The low R_{ON} (130mΩ) minimizes the device power dissipation when driving a wide range of output load current up to 2A when both channels are enabled or 3A when only one channel is enabled.

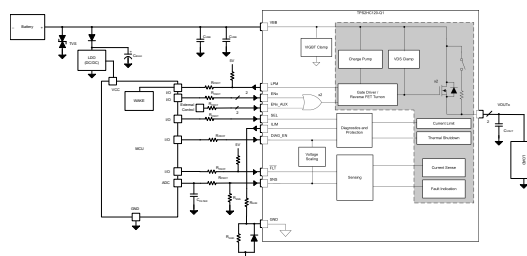
The device integrates protection features such as thermal shutdown, output clamp, and current limit. These features improve system robustness during fault events such as short circuit. TPS2HC120-Q1 implements a selectable current limiting circuit that improves the reliability of the system by reducing inrush current when driving large capacitive loads and minimizing overload current. The device offers 10 selectable current limit settings (0.25A to 4.7A) based on the external resistor used on the ILIM pin. The device also provides an accurate load current sense that allows for improved load diagnostics such as overload and open-load detection, which enables better predictive maintenance.

TPS2HC120-Q1 is available in a 28-pin, 4.9mm × 7.1mm HVSSOP leaded package with 0.5mm pin pitch minimizing the PCB footprint.

Package Information

PART NUMBER	PACKAGE ⁽¹⁾⁽²⁾	PACKAGE SIZE ⁽³⁾
TPS2HC120-Q1	DGQ (HVSSOP, 28)	4.90mm × 7.10mm

- (1) See also [Section 4](#).
- (2) For more information, see [Section 11](#)
- (3) The package size (length × width) is a nominal value and includes pins, where applicable.



Typical Application Schematic



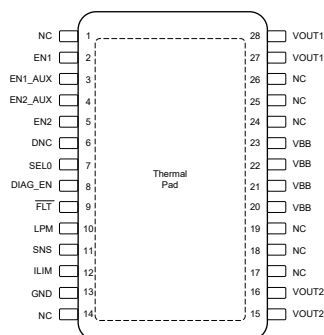
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4 Device Comparison Table

PART NUMBER	BEHAVIOR AFTER THERMAL FAULT
TPS2HC120A-Q1	LATCH off the faulted channel after thermal fault. Toggle EN to re-enable the specific channel.
TPS2HC120B-Q1	Auto-retry after thermal fault.

5 Pin Configuration and Functions



NC – No internal connection.

DNC – With internal connection. Do not connect externally.

Figure 5-1. DGQ Package, 28-Pin HVVSOP (Top View)

See [Section 8](#) for full list of recommended components.

Table 5-1. Pin Functions

PIN		TYPE	DESCRIPTION
NO.	NAME		
1, 14, 17, 18, 19, 24, 25, 26	NC	N/A	No internal connection.
2	EN1	Input	Input control for channel 1 activation, internal pulldown.
3	EN1_AUX	Input	Auxiliary input control for channel 1 activation, internal pulldown. Internally OR'd with EN1. Connect to GND if not using.
4	EN2_AUX	Input	Auxiliary input control for channel 2 activation, internal pulldown. Internally OR'd with EN2. Connect to GND if not using.
5	EN2	Input	Input control for channel 2 activation, internal pulldown.
6	DNC	—	Leave floating.
7	SEL0	Input	SNS channel-selection low bit; internal pulldown.
8	DIAG_EN	Input	Enable-disable pin for diagnostics, internal pulldown.
9	FLT	Output	Open drain fault output. Referred to as $\overline{\text{FLT}}$, or fault pin. Recommended 5-10k Ω pullup resistor
10	LPM	Output	Open drain LPM status pin. Pulled high by external supply if the device is in LPM or SLEEP state. Pulled low internally when device is in ACTIVE mode. Recommended 5-10k Ω pullup resistor.
11	SNS	Output	SNS current output
12	ILIM	Output	Adjustable current limit. Connect a resistor to chip GND, SHORT the pin to chip GND, or leave the pin OPEN to set the current limit value.
13	GND	Power	Ground of device. Connect to resistor- diode ground network to have reverse battery protection.
15,16	VOUT2	Power	Output of channel 2 of the high side switch, connected to load.
20, 21, 22, 23	VBB	Power	Power supply.
27,28	VOUT1	Power	Output of channel 1 of the high side switch, connected to load.
Thermal Pad	Pad	—	Thermal Pad, internally shorted to ground.

6 Specifications

6.1 Absolute Maximum Ratings

Over operating free-air temperature range (unless otherwise noted)⁽¹⁾

		MIN	MAX	UNIT
Maximum continuous supply voltage, V_{BB}			28	V
Load dump voltage, V_{LD}	ISO16750-2:2010(E)		35	V
Reverse Polarity Voltage	Maximum duration of 3 minutes and with the application circuit	-18		V
Enable pin current, I_{ENx}		-0.5	20	mA
Enable pin voltage, V_{ENx}		-1.5	5.5	V
Diagnostic Enable pin current, I_{DIAG_EN}		-0.5	20	mA
Diagnostic Enable pin voltage, V_{DIAG_EN}		-1.5	5.5	V
Sense pin current, I_{SNS}		-150	10	mA
Sense pin voltage, V_{SNS}		-1.5	5.5	V
SEL pin current, I_{SEL}		-0.5	20	mA
SEL pin voltage, V_{SEL}		-1.5	5.5	V
$\overline{FLT}$ pin current, I_{FLT}		-30	2.5	mA
$\overline{FLT}$ pin voltage, V_{FLT}		-0.3	5.5	V
$\overline{LPM}$ pin current, I_{LPM}		-30	2.5	mA
$\overline{LPM}$ pin voltage, V_{LPM}		-0.3	5.5	V
ILIM pin current, I_{ILIM}	ILIM pin current, I_{ILIM}	-0.5	20	mA
ILIM pin voltage, V_{ILIM}	ILIM pin voltage, V_{ILIM}	-1.5	5.5	V
Reverse ground current, I_{GND}	$V_{BB} < 0$ V	-50		mA
Maximum Energy Dissipation, single Pulse, E_{AS}	Single pulse, $L_{OUT} = 5.5$ mH, $T_{J,start} = 125^{\circ}\text{C}$, $V_{BB} = 24$ V, $I_{OUT} = 1.5$ A		16 ⁽²⁾	mJ
Maximum Energy Dissipation, repetitive Pulse, E_{AR}	Repetitive pulse, $L_{OUT} = 5.5$ mH, $T_{J,start} = 125^{\circ}\text{C}$, $V_{BB} = 24$ V, $I_{OUT} = 1.5$ A, 1M cycles		5.6 ⁽²⁾	mJ
Maximum junction temperature, T_J			150	$^{\circ}\text{C}$
Storage temperature, T_{stg}		-65	150	$^{\circ}\text{C}$

- (1) Operation outside the Absolute Maximum Ratings may cause permanent device damage. Absolute Maximum Ratings do not imply functional operation of the device at these or any other conditions beyond those listed under Recommended Operating Conditions. If used outside the Recommended Operating Conditions but within the Absolute Maximum Ratings, the device may not be fully functional, and this may affect device reliability, functionality, performance, and shorten the device lifetime.
- (2) For further details, see the section regarding switch-off of an inductive load.

6.2 ESD Ratings

			VALUE	UNIT
$V_{(ESD)}$	Electrostatic discharge ⁽¹⁾	Human-body model (HBM), per AEC Q100-002 Classification Level 2 ⁽²⁾	± 2000	V
		VBB and VOUT	± 4000	
		Charged-device model (CDM), per AEC Q100-011 Classification Level C5	± 750	

- (1) All ESD strikes are with reference from the pin mentioned to GND
- (2) AEC-Q100-002 indicates that HBM stressing shall be in accordance with the ANSI/ESDA/JEDEC JS-001 specifications.

6.3 Recommended Operating Conditions

over operating free-air temperature range (unless otherwise noted) ⁽¹⁾Digital input pins are EN1, EN2, EN1_AUX, EN2_AUX, SEL, DIAG_EN.

		MIN	MAX	UNIT
V _{VBB_NOM}	Nominal supply voltage ⁽¹⁾	6	18	V
V _{VBB_EXT}	Extended supply voltage ⁽²⁾	3	28	V
V _{VBB_SC}	Short circuit supply voltage capability		28	V
V _{DIO}	All digital output pin voltage	0	5.5	V
V _{DIN}	All digital input pin voltage	–1	5.5	V
T _A	Operating free-air temperature	–40	125	°C

(1) All operating voltage conditions are measured with respect to device GND

(2) Device will function within extended operating range, however some parametric values might not apply.

6.4 Thermal Information

THERMAL METRIC ⁽¹⁾⁽²⁾		TPS2HC120-Q1	UNIT
		DGQ (HVSSOP)	
		28 PINS	
R _{θJA}	Junction-to-ambient thermal resistance	33.5	°C/W
R _{θJC(top)}	Junction-to-case (top) thermal resistance	34.2	°C/W
R _{θJB}	Junction-to-board thermal resistance	11.3	°C/W
ψ _{JT}	Junction-to-top characterization parameter	1.9	°C/W
ψ _{JB}	Junction-to-board characterization parameter	11.3	°C/W
R _{θJC(bot)}	Junction-to-case (bottom) thermal resistance	2.9	°C/W

(1) For more information about traditional and new thermal metrics, see the [SPRA953](#) application report.

(2) The thermal parameters are based on a 4-layer PCB according to the JESD51-5 and JESD51-7 standards.

6.5 Electrical Characteristics

V_{BB} = 6 V to 18 V, T_J = –40°C to 150°C (unless otherwise noted); Typical application is 13.5V, 1A, R_{ILIM} = Open (unless otherwise specified). Digital input pins are EN1, EN2, EN1_AUX, EN2_AUX, SEL0, DIAG_EN.

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
INPUT VOLTAGE AND CURRENT						
V _{UVLOR}	V _{BB} undervoltage lockout rising	Measured with respect to the GND pin of the device	3.2	3.6	4.0	V
V _{UVLOF}	V _{BB} undervoltage lockout falling		2.5	2.75	3.0	V
V _{Clamp}	VDS clamp voltage	T _J = 25°C	35		43	V
		T _J = –40°C to 150°C	34		45	V
V _{OUTClamp}	VOUT clamp voltage	T _J = –40°C to 150°C	–31		–23	V
I _Q	Quiescent current all channels enabled	V _{BB} ≤ 28V, V _{EN} = 5V, V _{DIAG_EN} = 5V, I _{OUTx} = 0A		2.8	4.6	mA
I _{Q_DIAG_DIS}	Quiescent current channel enabled diagnostic disabled	V _{BB} ≤ 28V, V _{EN} = 5V, V _{DIAG_EN} = 0V, I _{OUTx} = 0A		3.8	4.3	mA
I _{SB}	Current consumption in standby mode	V _{BB} ≤ 18V, I _{SNS} = 0mA, V _{ENx} = 0V, V _{DIAG_EN} = 5V, V _{OUT} = 0V		3.8	4.6	mA
t _{STBY}	Delay time to remain in standby mode before entering sleep mode ⁽¹⁾	V _{ENx} = V _{DIAG_EN} = 5V to 0V	15	20	25	ms

6.5 Electrical Characteristics (continued)

$V_{BB} = 6\text{ V to }18\text{ V}$, $T_J = -40^\circ\text{C to }150^\circ\text{C}$ (unless otherwise noted); Typical application is 13.5V, 1A, $R_{ILIM} = \text{Open}$ (unless otherwise specified). Digital input pins are EN1, EN2, EN1_AUX, EN2_AUX, SEL0, DIAG_EN.

PARAMETER		TEST CONDITIONS		MIN	TYP	MAX	UNIT
I _{SLEEP}	Sleep current (total device leakage including MOSFET channels)	V _{BB} ≤ 18V, V _{ENx} = V _{DIAG_EN} = 0V, V _{OUT} = 0V	T _J = 25°C			0.5	μA
			T _J = 85°C			1.5	μA
			T _J = 150°C		0.7	2	μA
I _{OUT(standby)}	Output leakage current per channel in Standby ⁽¹⁾	V _{BB} ≤ 18V, V _{ENx} = V _{DIAG_EN} = 0V, V _{OUT} = 0V, V _{OUT} to GND	T _J = 25°C			6	μA
			T _J = 150°C			10	μA
I _{OUT(sleep)}	Output leakage current per channel in Sleep	V _{BB} ≤ 18V, V _{ENx} = V _{DIAG_EN} = 0V, V _{OUT} = 0V, V _{OUT} to GND	T _J = 25°C		0.01	0.1	μA
			T _J = 85°C			0.5	μA
			T _J = 150°C		0.2	1	μA
I _L NOM	Continuous load current per channel	Both channels enabled	T _J = 85°C		2		A
		One channel enabled			3		A
RON CHARACTERISTICS							
R _{ON}	On-resistance	5V < V _{BB} ≤ 28V, I _{OUT} = 1 A	T _J = 25°C		120		mΩ
			T _J = 150°C			250	
		3V ≤ V _{BB} ≤ 5V, I _{OUT} =1 A	T _J = 25°C			175	
			T _J = 150°C			280	
ΔR _{ON}	Percentage difference in On-state resistance between channels ⁽¹⁾	5V < V _{BB} ≤ 28V, I _{OUT} = 1A	T _J = −40°C to 150°C		0.5	5	%
R _{ON(REV)}	On-resistance during reverse polarity	−18V ≤ V _{BB} ≤ −6V	T _J = 25°C		120		mΩ
			T _J = 150°C			250	mΩ
V _F	Drain-to-source diode voltage	V _{EN} = 0V I _{OUT} = −0.1A			0.8	1	V
CURRENT SENSE CHARACTERISTICS							
K _{SNS}	Current sense ratio I _{OUT} / I _{SNS}	I _{OUT} = 1A			1030		
I _{SNSI}	Current sense current and accuracy ⁽²⁾	V _{EN} = V _{DIAG_EN} = 5V	I _{OUT} = 2A		1.9		mA
				−4		3	%
			I _{OUT} = 1.5A		1.43		mA
				−4		3	%
			I _{OUT} = 750mA		0.72		mA
				−4		3	%
			I _{OUT} = 300mA		0.29		mA
				−5		5	%
			I _{OUT} = 100mA		0.1		mA
				−12		12	%
			I _{OUT} = 75mA		0.072		mA
				−16		16	%
			I _{OUT} = 30mA		0.03		mA
				−35		35	%
			I _{OUT} = 15mA		0.014		mA
				−50		50	%
			I _{OUT} =10mA		0.0095		mA
				−80		80	%

6.5 Electrical Characteristics (continued)

$V_{BB} = 6\text{ V to }18\text{ V}$, $T_J = -40^\circ\text{C to }150^\circ\text{C}$ (unless otherwise noted); Typical application is 13.5V, 1A, $R_{ILIM} = \text{Open}$ (unless otherwise specified). Digital input pins are EN1, EN2, EN1_AUX, EN2_AUX, SEL0, DIAG_EN.

PARAMETER		TEST CONDITIONS		MIN	TYP	MAX	UNIT
SNS CHARACTERISTICS							
V _{SNSFH}	V _{SNS} fault high-level	V _{DIAG_EN} = 5V R _{SNS} = 1kΩ		4.5	4.85	5.2	V
		V _{DIAG_EN} = 3.3V R _{SNS} = 1kΩ		3.2	3.55	3.9	V
		V _{DIAG_EN} = V _{IH} (1.8V) R _{SNS} = 1kΩ		3.2	3.55	3.9	V
I _{SNSFH}	I _{SNS} fault high-level	V _{DIAG_EN} > V _{IH,DIAG_EN}		4.5		6	mA
I _{SNSleak_EN}	Leakage current on SNS pin (sensing enabled)			-11	-0.5	11	μA
I _{SNSleak_DIS}	Leakage current on SNS pin (sensing disabled)			-1	-0.01	1	μA
V _{BB_ISNS}	V _{BB} headroom needed for full current sense and fault functionality ⁽¹⁾	V _{DIAG_EN} = 3.3V	Measure with respect to GND pin of device	5			V
		V _{DIAG_EN} = 5V		6.5		V	
CURRENT LIMIT CHARACTERISTICS							
I _{CL}	I _{CL} setting ⁽³⁾	R _{ILIM} > 87kΩ (ILIM open)		4	4.7	5.6	A
		R _{ILIM} < 1.1kΩ (ILIM short to ground)		1.9	2.1	2.4	
		R _{ILIM} = 2.37kΩ to 2.61kΩ		1.7	1.9	2.1	
		R _{ILIM} = 4.64kΩ to 5.11kΩ		1.5	1.68	1.85	
		R _{ILIM} = 9.31kΩ to 10.5kΩ		1.3	1.44	1.6	
		R _{ILIM} = 15.8kΩ to 17.3kΩ		1.1	1.21	1.31	
		R _{ILIM} = 22.1kΩ to 24.3kΩ		0.85	1	1.1	
		R _{ILIM} = 29.5kΩ to 32.4kΩ		0.65	0.75	0.85	
		R _{ILIM} = 41.2kΩ to 45.9kΩ		0.4	0.5	0.6	
R _{ILIM} = 54.9kΩ to 60.4kΩ		0.19	0.25	0.32			
I _{CL_ENPS}	Peak current enabling into permanent short ⁽¹⁾	T _J = -40°C to 150°C	Load = 5μH +100mΩ	1.5 × I _{CL}	2 × I _{CL}	2.25 × I _{CL}	A
I _{CL_LINPK}	Linear Mode peak ⁽¹⁾	T _J = -40°C to 150°C dI/dt < 0.01 A/ms	I _{ILIM} = 0.25A to 2.1A	I _{CL}	1.12 × I _{CL}	1.4 × I _{CL}	A
I _{OVCR}	OVCR Peak current when short is applied while switch enabled ⁽¹⁾	T _J = -40°C to 150°C	Load = 5μH +100mΩ, R _{ILIM} = Open	8	11	16.5	A
t _{OVCR}	OVCR reaction time when short is applied while switch enabled ⁽¹⁾	T _J = -40°C to 150°C	Load = 5μH +100mΩ	0.5	1	2	μs
FAULT CHARACTERISTICS							
R _{PU}	Open-load (OL) detection internal resistor	V _{EN} = 0 V, V _{DIAG_EN} = 5V		100	135	175	kΩ
t _{OL}	Open-load (OL) detection deglitch time	V _{EN} = 0V, V _{DIAG_EN} = 5V, When V _{BB} – V _{OUT} < V _{OL,off} , duration longer than t _{OL} . Open load detected.			300	500	μs
V _{OL,off}	Open-load (OL) detection voltage	V _{EN} = 0V, V _{DIAG_EN} = 5V		1		1.5	V
t _{OL1}	OL and STB indication-time from EN falling	V _{EN} = 5V to 0V, V _{DIAG_EN} = 5V I _{OUT} = 0mA, V _{OUT} = V _{BB} – V _{OL,off}				500	μs
t _{OL2}	OL and STB indication-time from DIA_EN rising	V _{EN} = 0V, V _{DIAG_EN} = 0V to 5V I _{OUT} = 0mA, V _{OUT} = V _{BB} – V _{OL,off}				600	μs
T _{ABS}	Thermal shutdown for CHx ⁽¹⁾			162	177	192	°C
T _{HYS}	CHx Thermal shutdown hysteresis ⁽¹⁾					30	°C

6.5 Electrical Characteristics (continued)

$V_{BB} = 6\text{ V to }18\text{ V}$, $T_J = -40^\circ\text{C to }150^\circ\text{C}$ (unless otherwise noted); Typical application is 13.5V, 1A, $R_{ILIM} = \text{Open}$ (unless otherwise specified). Digital input pins are EN1, EN2, EN1_AUX, EN2_AUX, SEL0, DIAG_EN.

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT	
T _{REL}	CHx Relative thermal shutdown		80			°C	
t _{FAULT_FLT}	Fault indication-time	V _{DIAG_EN} = 5V Time between fault and FLT asserting			60	μs	
t _{FAULT_SNS}	Fault indication-time	V _{DIAG_EN} = 5V Time between fault and I _{SNS} settling at V _{SNSFH}			60	μs	
t _{RETRY}	Retry time	Time from fault shutdown until switch re-enable (thermal shutdown).	1	2	3	ms	
LOW POWER MODE							
I _{LPM,enter}	Load current level for entry to LPM	t > t _{STBY}	83	110	137	mA	
I _{LPM,exit}	Load current level for exit of LPM		130	165	200	mA	
R _{DSON,LPM}	RDSON in Low Power Mode	50mA I _{LOAD}	130			mΩ	
I _{QLPM}	Quiscent current per channel in LPM with one channels enabled ⁽¹⁾	I _{LOAD} = 0 mA, T _J = -40°C to 150°C	33			60	μA
	Quiscent current per channel in LPM with all channels enabled ⁽¹⁾	I _{LOAD} = 0 mA, T _J = -40°C to 150°C	20			33	μA
t _{LPM}	LPM Transistion indication-time ⁽¹⁾	Device in LPM transistioning out time between current increase and LPM asserting				50	μs
t _{WAKE}	Recovery/Exit time from LPM ⁽¹⁾	Device in LPM transistioning out time between wake interrupt and LPM asserting				50	μs
I _{PKLPM,SC}	Short circuit threshold for immediate shut-off during LPM mode	I _{LIM} ≤ 2.1A	1.6×I _{LIM}				
		R _{ILIM} = OPEN	3.6			A	
DIGITAL INPUT PIN CHARACTERISTICS							
V _{IL, DIN}	Input voltage low-level	No GND Network				0.8	V
V _{IH, DIN}	Input voltage high-level	No GND Network	1.5				V
V _{IHYS, DIN}	Input voltage hysteresis		100				mV
R _{PD_DIN}	Internal pulldown resistor for ENx, ENx_AUX, DIAG_EN		0.7	1	1.3		MΩ
	Internal pulldown resistor for SEL		0.7	1	1.3		MΩ
I _{IH, DIN}	Input current high-level for SEL	V _{DINx} = 5.5V				10	μA
	Input current high-level for DIAG_EN	V _{DIAG_EN} = 5.5V				30	
	Input current high-level for ENx	V _{ENx} = 5.5V				30	
DIGITAL OUTPUT PIN CHARACTERISTICS							
V _{LPM}	LPM low output voltage	I _{LPM} = 2mA				0.4	V
V _{FLT}	FLT low output voltage	I _{FLT} = 2mA				0.4	V

- (1) Parameter specified by design; not subject to production test.
- (2) Current sense current accuracy specification includes error contribution from leakage current on SNS pin in sensing enabled state.
- (3) Effective RILIM resistance, including tolerances, must fall within the specified RILIM resistance ranges.

6.6 SNS Timing Characteristics

$V_{BB} = 6V$ to $18V$, $T_J = -40^{\circ}C$ to $+150^{\circ}C$ (unless otherwise noted)

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
SNS TIMING - CURRENT SENSE						
$t_{SNSION1}$	Settling time from rising edge of DIAG_EN 50% of V_{DIAG_EN} to 90% of settled $ISNS^{(1)}$	$V_{EN} = 5V$, $V_{DIAG_EN} = 0V$ to $5V$ $R_{SNS} = 1k\Omega$, $I_L = 15mA$			80	μs
		$V_{EN} = 5V$, $V_{DIAG_EN} = 0V$ to $5V$ $R_{SNS} = 1k\Omega$, $I_L = 30mA$			60	μs
		$V_{ENx} = 5V$, $V_{DIAG_EN} = 0V$ to $5V$ $R_{SNS} = 1k\Omega$, $I_L = 1A$			30	μs
$t_{SNSION2}$	Settling time from rising edge of EN and DIAG_EN 50% of V_{DIAG_EN} , V_{ENx} to 90% of settled $ISNS^{(1)}$	$V_{ENx} = V_{DIAG_EN} = 0V$ to $5V$ $V_{BB} = 13.5V$ $R_{SNS} = 1k\Omega$, $R_{LOAD} = 1k\Omega$			150	μs
		$V_{ENx} = V_{DIAG_EN} = 0V$ to $5V$ $V_{BB} = 13.5V$ $R_{SNS} = 1k\Omega$, $R_{LOAD} = 20\Omega$			150	μs
$t_{SNSION3}$	Settling time from rising edge of EN with DIAG_EN HI; 50% of V_{DIAG_EN} V_{EN} to 90% of settled $ISNS^{(1)}$	$V_{EN} = 0V$ to $5V$, $V_{DIAG_EN} = 5V$ $V_{BB} = 13.5V$ $R_{SNS} = 1k\Omega$, $R_{LOAD} = 20\Omega$			150	μs
$t_{SNSIOFF}$	Settling time from falling edge of DIAG_EN ⁽¹⁾	$V_{EN} = 5V$, $V_{DIAG_EN} = 5V$ to $0V$ $V_{BB} = 13.5V$ $R_{SNS} = 1k\Omega$, $R_L = 20\Omega$			20	μs
$t_{SETTLEH}$	Settling time from rising edge of load step ⁽¹⁾	$V_{EN} = 5V$, $V_{DIAG_EN} = 5V$ $R_{SNS} = 1k\Omega$, $I_{OUT} = 10mA$ to $1A$			20	μs
$t_{SETTLEL}$	Settling time from falling edge of load step ⁽¹⁾	$V_{EN} = 5V$, $V_{DIAG_EN} = 5V$ $R_{SNS} = 1k\Omega$, $I_{OUT} = 1A$ to $10mA$			20	μs
t_{SELx}	Multi-sense transition delay from channel to channel ⁽¹⁾	$V_{EN} = 5V$, $V_{DIAG_EN} = 5V$ $R_{SNS} = 1k\Omega$, $I_{OUT1} = 1A$ to $I_{OUT2} = 0.5A$			50	μs

(1) Parameter specified by design; not subject to production test.

6.7 Switching Characteristics

$V_{BB} = 13.5V$, $T_J = -40^{\circ}C$ to $+150^{\circ}C$ (unless otherwise noted)

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
t_{DR}	Channel Turn-on delay time (from Active)	$V_{BB} = 13.5V$, $R_L = 1k\Omega$ 50% of EN to 10% of V_{OUT}		30	55	μs
	Channel Turn-on delay time (from Sleep or LPM)			40	60	μs
t_{DF}	Channel Turn-off delay time (from Active)	$V_{BB} = 13.5V$, $R_L = 100\Omega$ 50% of EN to 90% of V_{OUT}		30	55	μs
	Channel Turn-off delay time (from LPM)	$V_{BB} = 13.5V$, $R_L = 1k\Omega$ 50% of EN to 90% of V_{OUT}		30	85	μs
SR_R	V_{OUT} rising slew rate	$V_{BB} = 13.5V$, 20% to 80% of V_{OUT} , $R_L = 100\Omega$	0.1	0.3	0.55	$V/\mu s$
SR_F	V_{OUT} falling slew rate	$V_{BB} = 13.5V$, 80% to 20% of V_{OUT} , $R_L = 100\Omega$	0.1	0.3	0.5	$V/\mu s$
t_{ON}	Channel Turn-on time (STANDBY DELAY to ACTIVE)	$V_{BB} = 13.5V$, $R_L = 100\Omega$ 50% of EN to 80% of V_{OUT}	30	50	100	μs
t_{OFF}	Channel Turn-off time (ACTIVE to STANDBY DELAY)	$V_{BB} = 13.5V$, $R_L = 100\Omega$ 50% of EN to 20% of V_{OUT}	30	70	145	μs

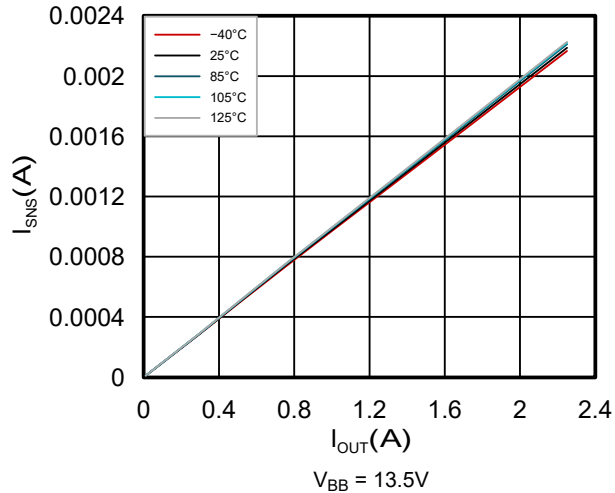
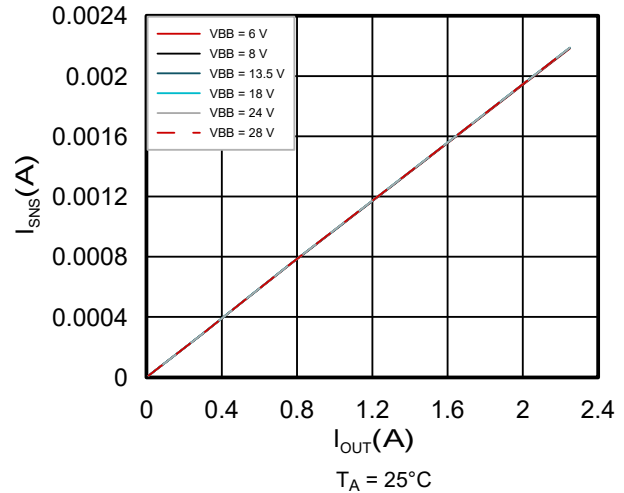
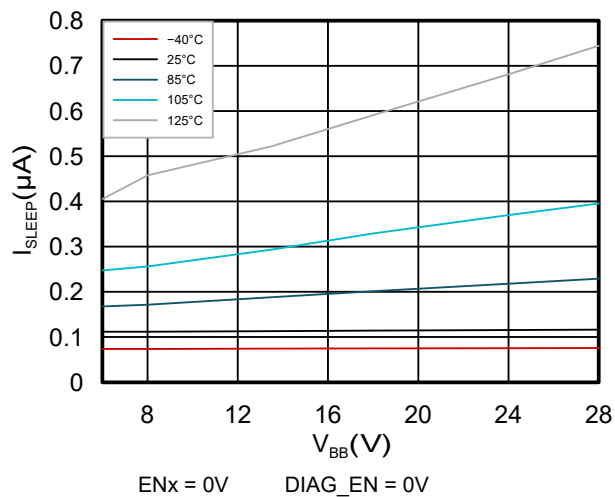
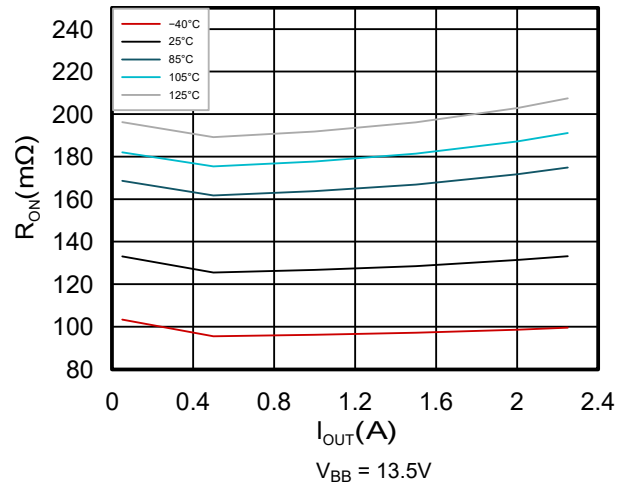
6.7 Switching Characteristics (continued)

$V_{BB} = 13.5\text{ V}$, $T_J = -40^\circ\text{C}$ to $+150^\circ\text{C}$ (unless otherwise noted)

PARAMETER	TEST CONDITIONS	MIN	TYP	MAX	UNIT
$t_{ON} - t_{OFF}$	Turn-on and off matching ⁽¹⁾	1ms enable pulse $V_{BB} = 13.5\text{V}$, $R_L = 100\Omega$	-40	40	μs
		200- μs enable pulse, $V_{BB} = 13.5\text{V}$, $R_L = 100\Omega$,	-40	40	μs
Δ_{PWM}	PWM accuracy - average load current ⁽¹⁾	200- μs enable pulse (1ms period), $V_{BB} = 13.5\text{V}$, $R_L = 100\Omega$	-25	25	%
		$\leq 500\text{Hz}$, 50% Duty cycle $V_{BB} = 13.5\text{V}$, $R_L = 100\Omega$	-12	12	%
E_{ON}	Switching energy losses during turn-on	$V_{BB} = 13.5\text{V}$, $R_L = 100\Omega$	0.2		mJ
E_{OFF}	Switching energy losses during turn-off	$V_{BB} = 13.5\text{V}$, $R_L = 100\Omega$	0.2		mJ

(1) Parameter specified by design; not subject to production test.

6.8 Typical Characteristics

Figure 6-1. I_{SNS} vs I_{OUT} Over TemperatureFigure 6-2. I_{SNS} vs I_{OUT} Over V_{BB} VoltageFigure 6-3. I_{SLEEP} vs V_{BB} Over TemperatureFigure 6-4. R_{ON} vs I_{OUT} Over Temperature

6.8 Typical Characteristics (continued)

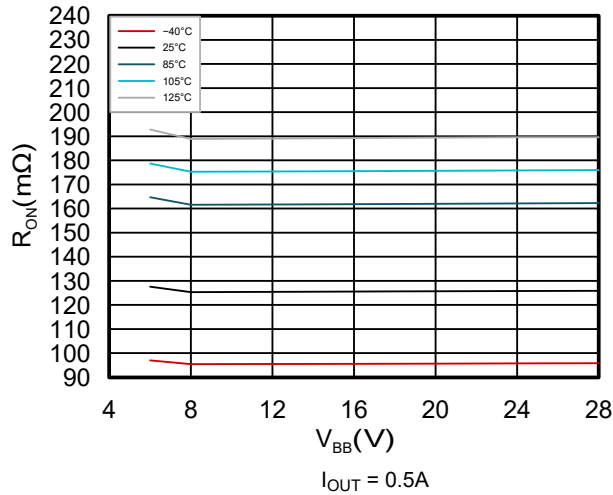


Figure 6-5. R_{ON} vs V_{BB} Over Temperature

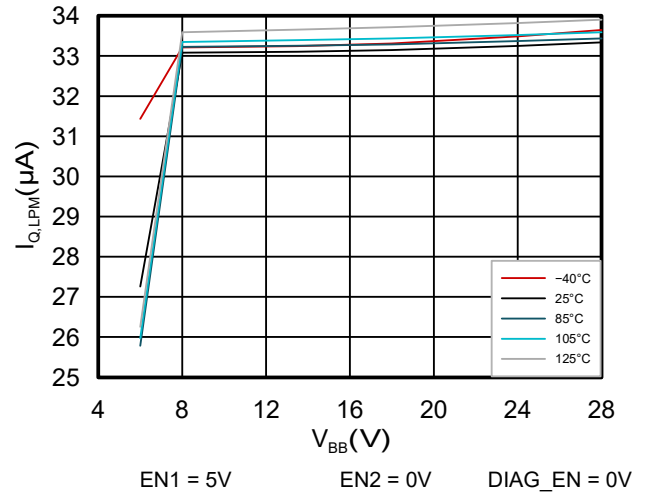


Figure 6-6. $I_{Q,LPM}$ vs V_{BB} Over Temperature When 1 Channel is Enabled

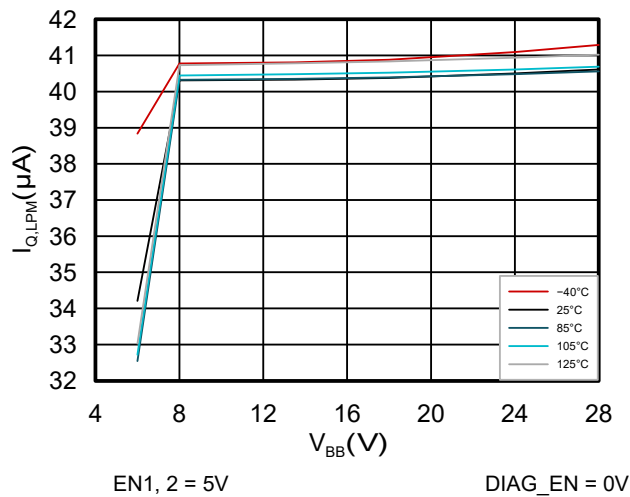


Figure 6-7. $I_{Q,LPM}$ vs V_{BB} Over Temperature When 2 Channels are Enabled

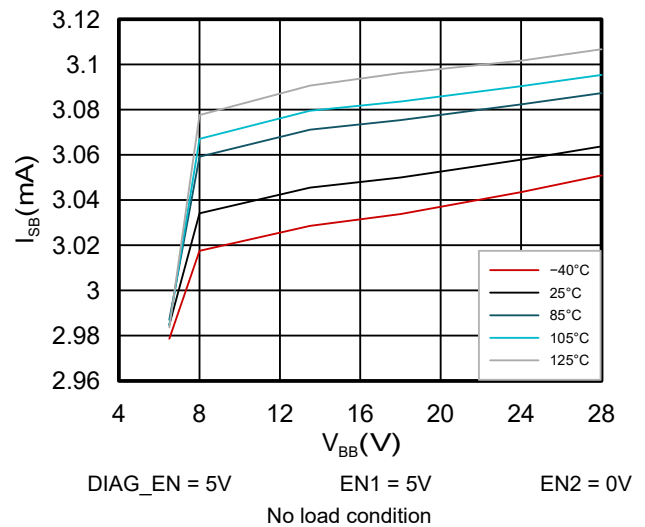


Figure 6-8. I_{SB} vs V_{BB} Over Temperature

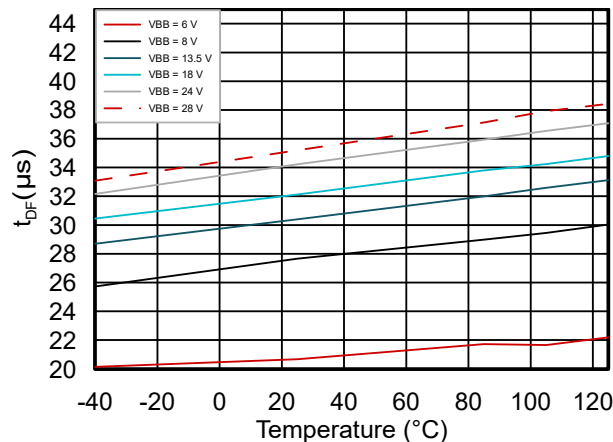


Figure 6-9. t_{DF} vs Temperature Over V_{BB} Voltage

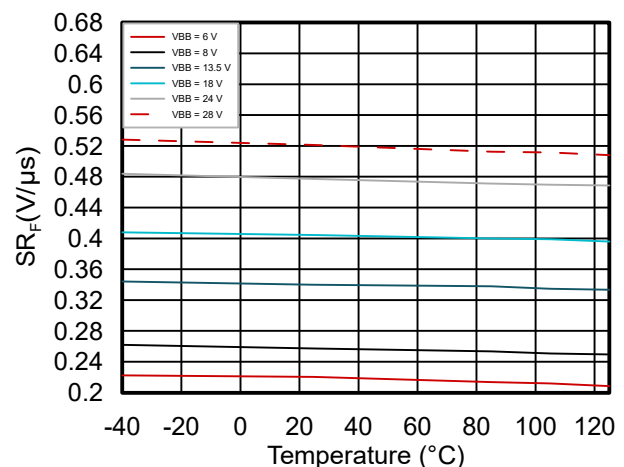


Figure 6-10. SR_F vs Temperature Over V_{BB} Voltage

6.8 Typical Characteristics (continued)

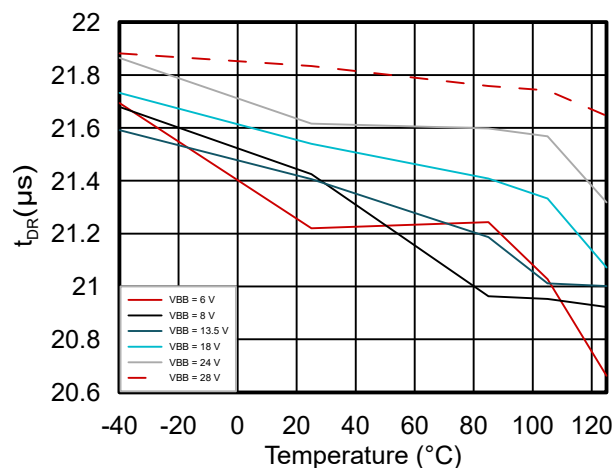
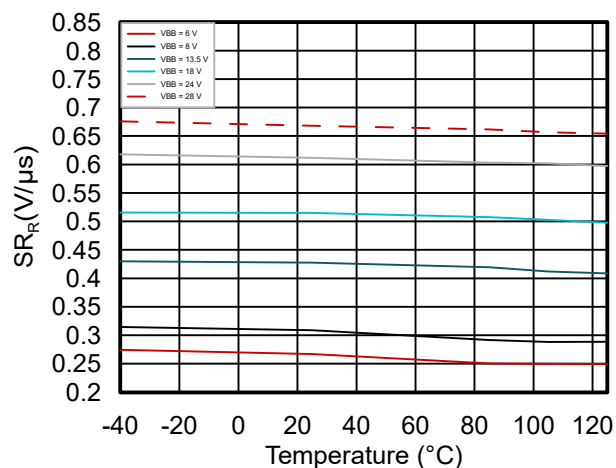
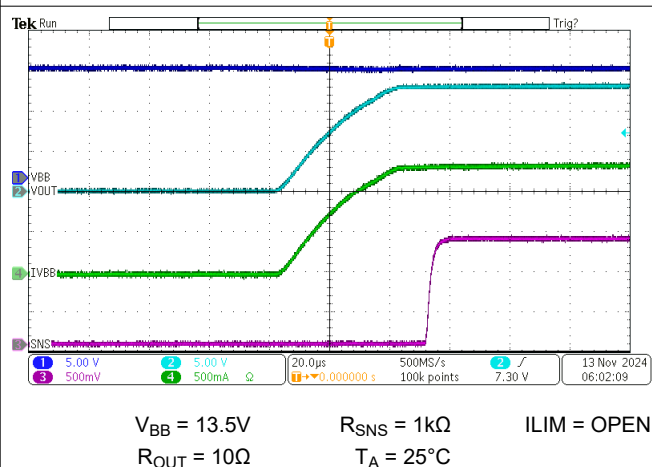
Figure 6-11. t_{DR} vs Temperature Over V_{BB} VoltageFigure 6-12. S_R vs Temperature Over V_{BB} Voltage

Figure 6-13. Switch Turn-On

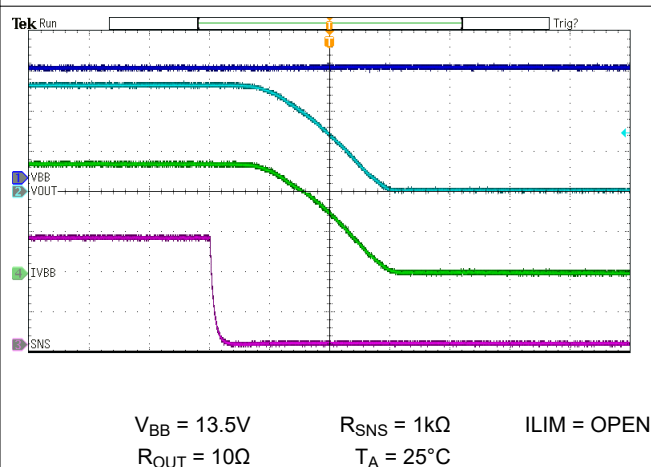


Figure 6-14. Switch Turn-Off

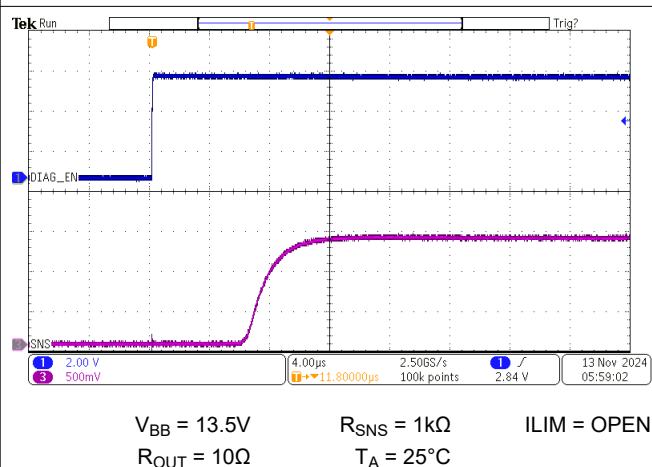
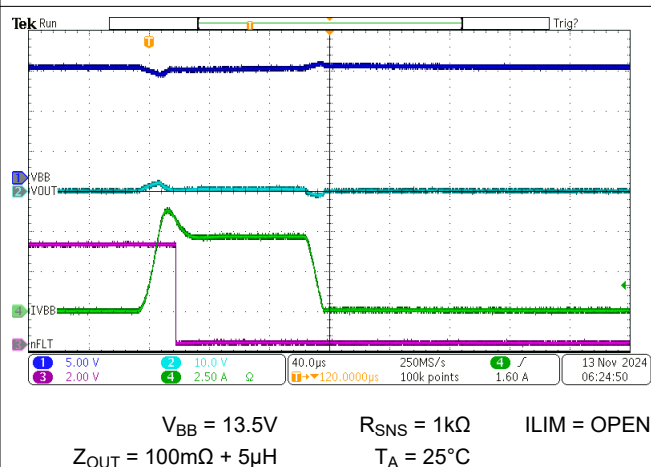
Figure 6-15. S_{NS} Pin Voltage With $DIAG_EN$ Turning ON

Figure 6-16. Permanent Short Behavior With ILIM Open

6.8 Typical Characteristics (continued)

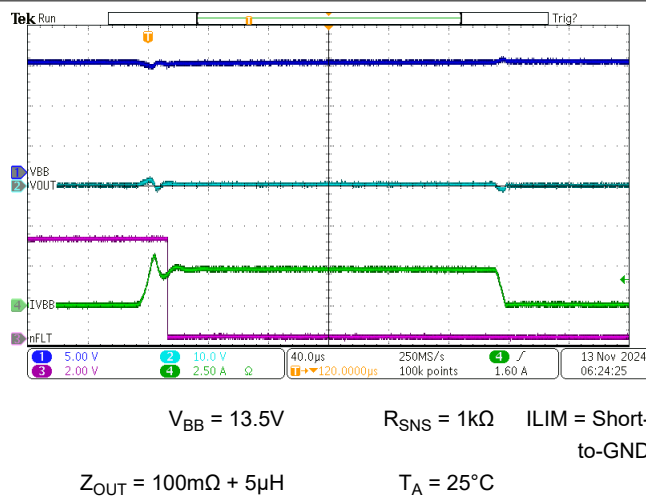


Figure 6-17. Permanent Short Behavior With ILIM Short-to-GND

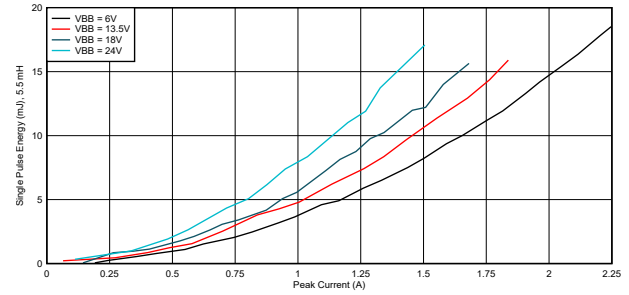


Figure 6-18. Single Pulse Inductive Energy, $L = 5.5mH$, $T_J = 125^\circ C$, $V_{BB} = 24V$, $I_{OUT} = 1.5A$

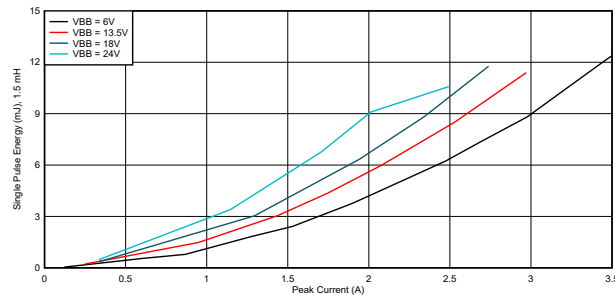


Figure 6-19. Single Pulse Inductive Energy, $L = 1.5mH$, $T_J = 125^\circ C$, $V_{BB} = 24V$, $I_{OUT} = 1.5A$

7 Detailed Description

7.1 Overview

The TPS2HC120-Q1 device is a smart high-side switch, with internal charge pump and dual-channel integrated NMOS power FETs. Full diagnostics and high-accuracy current-sense features enable intelligent control of the load. The adjustable current-limit function greatly improves the reliability of the whole system.

The device has logic pins to enable each of the two channels and a separate pin to enable the diagnostic output with SEL pin to select the channel to be output on the analog current SNS pin. The device also implements a FLT pin for use as an interrupt to the MCU. The digital input pins are synchronized with an internal clock, and therefore can exhibit jitter of a few microseconds due to the asynchronous external input signal.

The external high-accuracy current limit allows setting the current-limit value by applications. When overcurrent occurs, the device improves system reliability by clamping the inrush current effectively. The device also helps save system cost by reducing the size of PCB traces and connectors, and the capacity of the preceding power stage.

For inductive loads (relays, solenoids, valves), the device implements an active clamp between drain and source for protection. During the inductive switching-off cycle, both the energy of the power supply and the load are dissipated on the high-side switch. The device also optimizes the switching-off slew rate when the clamp is active, which helps the system design by keeping the effects of transient power and EMI to a minimum.

When the current consumptions on all channels are small, along with other requirements described in [Section 7.3.2.1](#), the device automatically enters low-power mode. This mode has ultra-low quiescent current consumption, and is applicable for loads that are active when the vehicle is off to preserve the battery. There is a dedicated LPM pin that indicates the mode of the device, and is useful as an interrupt signal to wake up the MCU.

The TPS2HC120-Q1 device is able to drive a wide variety of resistive, inductive, and capacitive loads, including low-wattage bulbs, LEDs, relays, solenoids, heaters, and sub-modules.

7.2 Functional Block Diagram

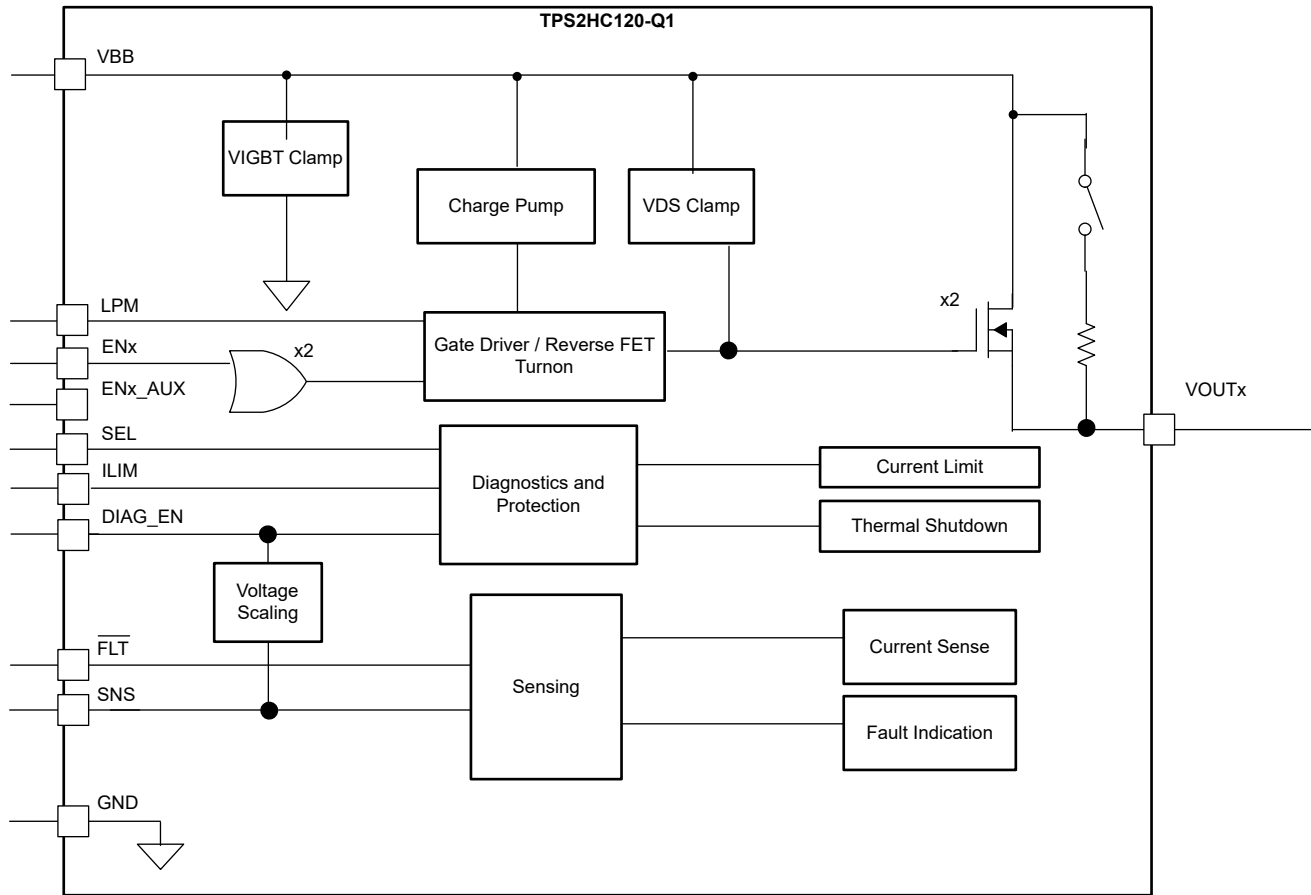


Figure 7-1. Functional Block Diagram

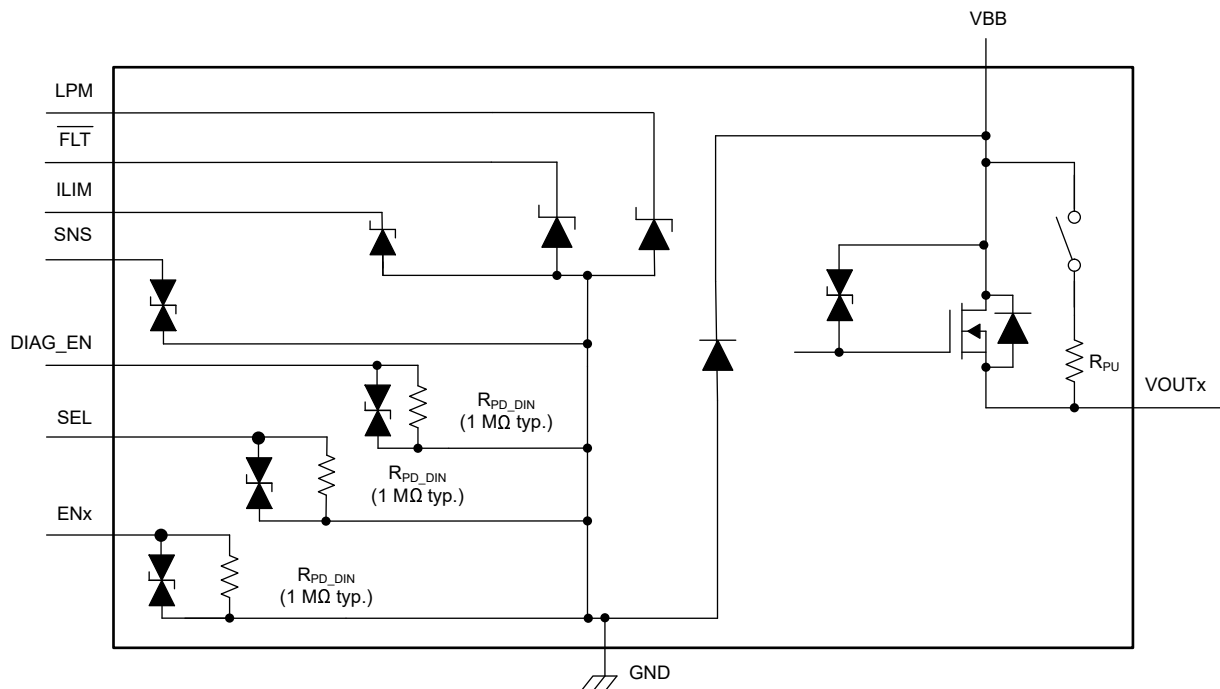


Figure 7-2. Internal Diode Diagram

7.3 Feature Description

7.3.1 Pin Current and Voltage Conventions

For reference purposes throughout the datasheet, the arrows in [Figure 7-3](#) show the current directions on the respective pins. The direction is used to indicate the polarities of current in [Specifications](#), but not to represent the actual current flow direction of each pin. All voltages are measured relative to the ground plane.

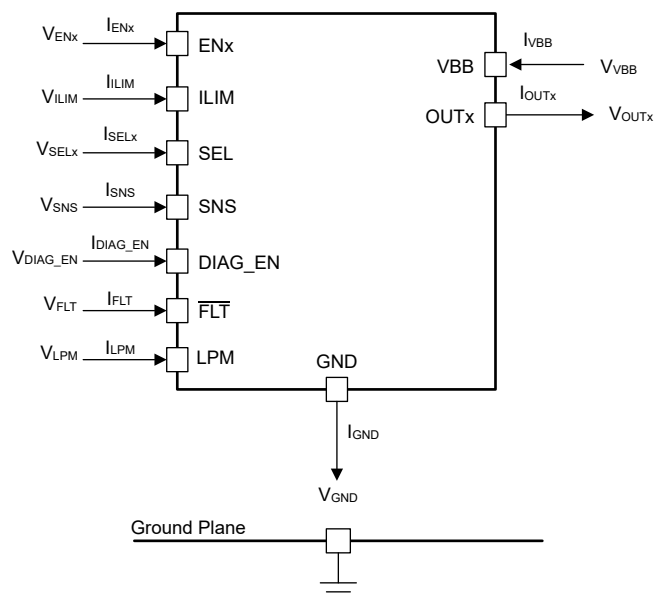


Figure 7-3. Voltage and Current Conventions

7.3.2 Low Power Mode

Low power mode (LPM) is designed to be able to still provide small amounts of current to loads without consuming much quiescent current. This type of feature is useful in power-at-all-time loads or to just generally reduce the amount of power dissipation from the supply. The quiescent current draw during this mode is defined in [Section 6.5](#) under $I_{Q,LPM}$. The TPS2HC120-Q1 can automatically enter and exit this mode by detecting that the load current is below $I_{LPM,enter}$ on all active channels, and then exits this mode when load current increases above $I_{LPM,exit}$. This section describes the entry, exit and protections mechanisms in this mode.

7.3.2.1 Entry Into LPM

When the load current going through the channel is below the $I_{LPM,enter}$ threshold on all active channels and diagnostics are turned off (DIAG_EN is low) for longer than t_{STBY} , the device automatically enters into LPM. This means that the digital core is turned off and the charge pump strength is reduced to reduce the quiescent current to $I_{Q,LPM}$.

All the requirements below need to be met for the device to enter the LPM automatically:

- $T_J < 125^{\circ}\text{C}$
- $V_{BB} \geq 6\text{V}$
- DIAG_EN is LOW
- At least one channel is ON
- All the ON channels have load currents $< I_{LPM,enter}$ per channel
- No EN pin toggling
- All the above conditions are true for time longer than t_{STBY}
 - During t_{STBY} , only the **output** of the OR'd ENx is monitored for the condition: "No EN pin toggling"

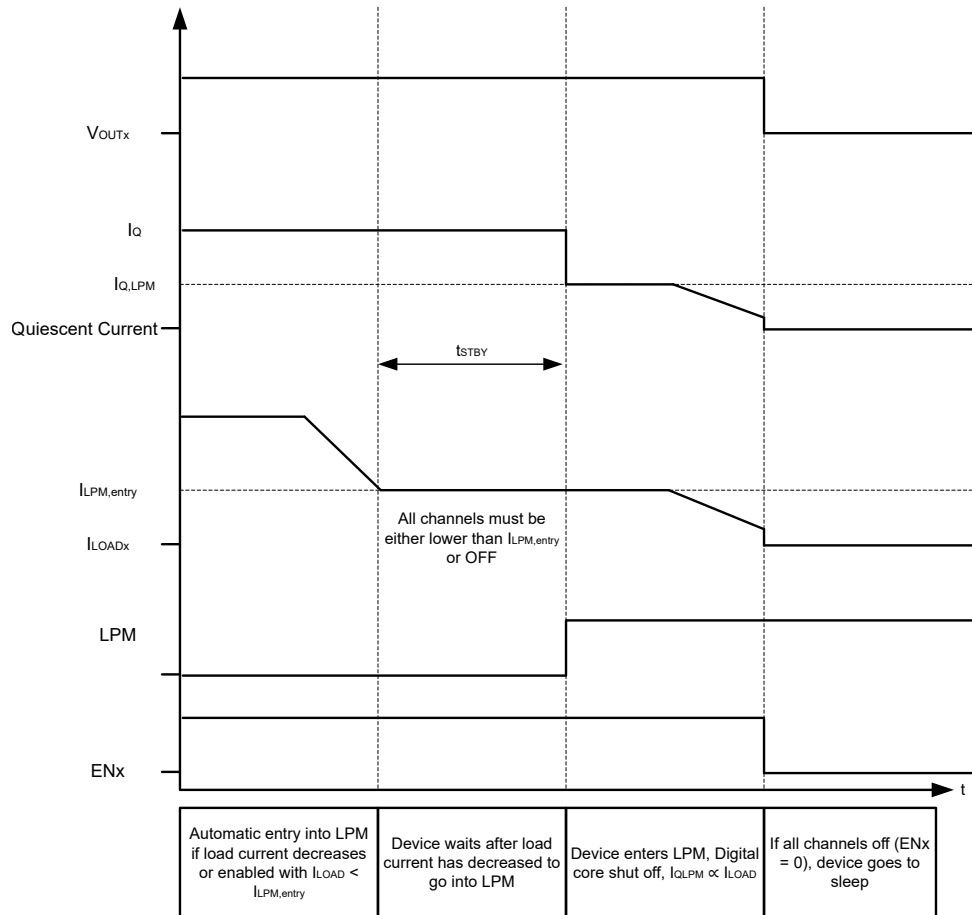


Figure 7-4. Entering LPM

7.3.2.2 During LPM

The quiescent current of the device during LPM, $I_{Q,LPM}$, is a function of how many channels are active and is proportional to the load current meaning that the lower the load current during this time, the lower the quiescent current is. Additionally, since the digital core is disabled, the diagnostics like current sensing or open load detection are not available during this mode. If diagnostics are desired, the DIAG_EN pin can be enabled to exit LPM and return the part back to normal operation. Once DIAG_EN is disabled the device goes back into LPM after t_{STBY} . Similarly, the current limit mechanism is not active in the same manner as by definition the minimum current limit is higher than the entry point of LPM. However, the short-circuit protection is still in place to protect the device.

Below is the summary of the behavior of the device during LPM:

- I_Q reduces to $I_{Q,LPM}$ per channel
- $R_{DS,ON}$ per channel increases to $R_{DS,ON,LPM}$
- No clamped current limit for overload conditions as the device exits the LPM first
- Short-circuit protection is in place to shut off the device if load current increases to $I_{PK,LPM,SC}$ during LPM
- No thermal shutdown protection

7.3.2.3 Exiting LPM

The device exits LPM if any of four conditions is met:

- Load current increases slowly: If the load current increases beyond $I_{LPM,exit}$ slowly, the device wakes up and pulls the LPM pin low to signal the device is no longer in low power mode. The output voltage droop is minimal.

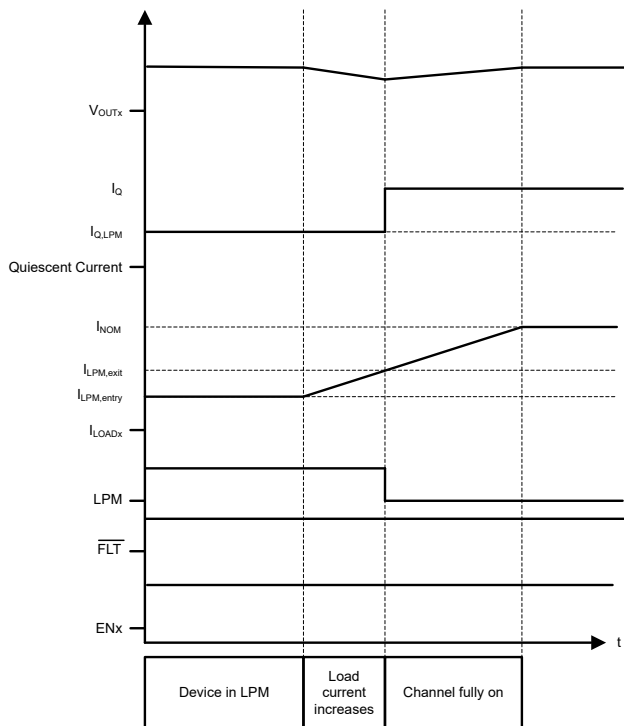


Figure 7-5. Exiting LPM With Load Current Slow Increase

- Load current increases rapidly (short-circuit): If the load current increases rapidly beyond $I_{PKLPM,SC}$, the device shuts down to protect itself and come back on within the t_{WAKE} time in normal operation with full functionality. As the part comes back on, LPM pin is pulled LOW to represent that the part has come out of LPM. The $\overline{FLT}$ pin continues to be pulled low if the fault is still present after exiting LPM.

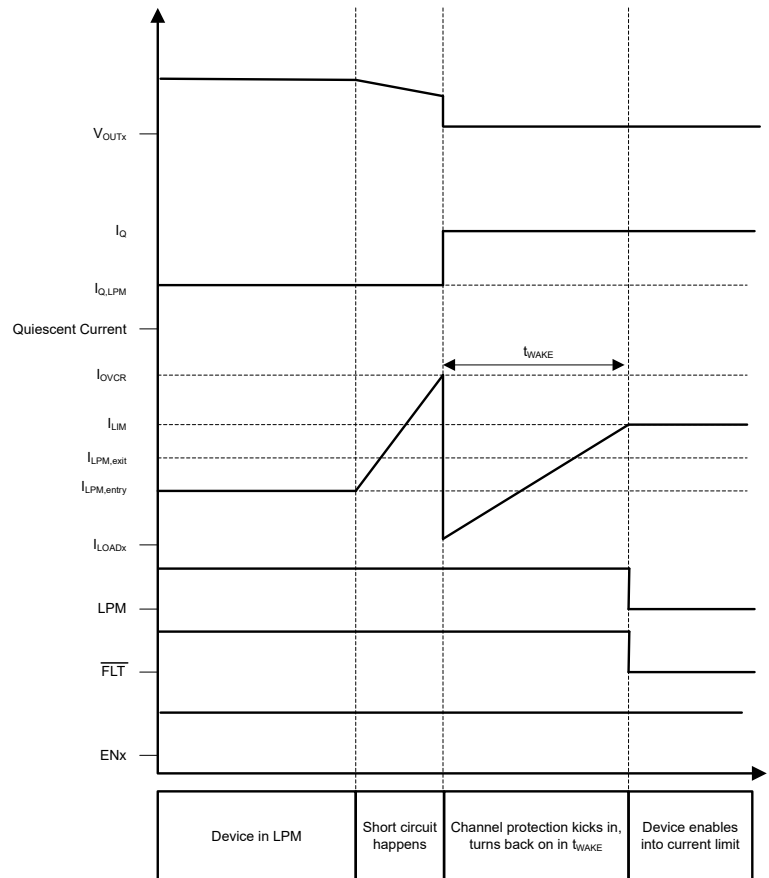


Figure 7-6. Exiting LPM With Rapid Load Current Increase (Short-Circuit)

- Any ENx is toggled (from ON to OFF or OFF to ON): If any channel is turned ON or turned OFF during LPM, the device wakes up and perform the desired action. **Additionally, any toggling of ENx_AUX wakes up the device, even if it does not cause an ON/OFF transition.** After the device wakes up, if the LPM entry conditions are still met, the part enters LPM again after t_{STBY} .
- DIAG_EN is turned ON: if DIAG_EN goes high, the device goes into the DIAGNOSTIC mode which fully turns on the part so that all of the functionality works as intended in the DIAGNOSTIC state. If DIAG_EN goes back low, with all LPM entry conditions are met, the part goes back into LPM after t_{STBY} .

Any time the device comes out of LPM to ACTIVE state, the LPM pin is pulled LOW. If the system needs to wake up when the device comes out of LPM, the LPM pin can be used to send a wake up signal to the MCU. Otherwise the LPM pin can be ignored.

7.3.3 Accurate Current Sense

The high-accuracy current-sense function is internally implemented, which allows a better real-time monitoring effect and more-accurate diagnostics without further calibration. A current mirror is used to source $1 / K_{SNS}$ of the load current, flowing out to the external resistor between the SNS pin and GND, and reflected as voltage on the SNS pin.

K_{SNS} is the ratio of the output current and the sense current. The accuracy values of K_{SNS} quoted in the *Electrical Characteristics* take into consideration temperature and supply voltage. Each device is internally calibrated while in production, so post-calibration by users is not required in most cases.

The maximum voltage out on the SNS pin is clamped to V_{SNSFH} , which is the fault voltage level. This voltage is made a function of the DIAG_EN voltage to confirm that it is not higher than what the system can tolerate. If DIAG_EN is between V_{IH} and 3.3V, the maximum output on the SNS pin is approximately 3.3V. However, if the voltage at DIAG_EN is above 3.3V, then the fault SNS voltage, V_{SNSFH} , tracks that voltage up to 5V. Tracking

is done because the GPIO voltage output that is powering the diagnostics through DIAG_EN is close to the maximum acceptable ADC voltage within the same microcontroller.

Therefore, select the sense resistor value, R_{SNS} , to maximize the range of currents needed to be measured by the system. The maximum usable R_{SNS} value is bounded by the ADC minimum acceptable voltage, $V_{ADC,min}$, for the smallest load current needed to be measured by the system, $I_{LOAD,min}$. Select the minimum acceptable R_{SNS} value so that the V_{SNS} voltage is less than the V_{SNSFH} value, allowing for the system to correctly determine faults.

The clamp on the SNS pin is enabled when DIAG_EN is low as well. So, if the application has tied SNS pins of multiple devices together, external multiplexers can be used to read individual SNS pin voltages. The multiplexers can be controlled by the DIAG_EN signal of individual devices.

In case a GND network is used for reverse polarity protection, the voltage drop across the GND network has to be taken into account to confirm that the SNS pin voltage does not exceed the maximum acceptable ADC voltage. For example, if the microcontroller is running at 3.3V and a GND network is used, the effective DIAG_EN voltage seen by the device is lowered by the amount of offset induced by the GND network, typically about 0.7V. As a result, the SNS pin clamps to about 3.3V plus the GND offset. External clamp diodes can be used to restrict the SNS pin voltage in such cases.

The difference between the maximum readable current through the SNS pin, $I_{LOAD,max} \times R_{SNS} / K_{SNS}$, and the V_{SNSFH} is called the headroom voltage, V_{HR} . The headroom voltage is determined by the system, the supply voltage and whether a ground network is used. The current sensing output voltage limitation due to V_{HR} starts at VBB approximately 2.6V + V_{SNS} when a GND network is used. In the case of a fault level, the voltage drop is smaller (approximately 1.5V), because when there is a fault, the internal SENSE FET is bypassed, which leads to lower headroom requirement. Without a ground network, the SNS pin voltage limitation due to V_{HR} starts at a lower VBB (by about 0.7V).

It is important to maintain a headroom so that there is a difference between the maximum readable current and a fault condition. Therefore, the minimum R_{SNS} value has to be the V_{SNSFH} minus the V_{HR} times the sense current ratio, K_{SNS} divided by the maximum load current the system must measure, $I_{LOAD,max}$. Use the following equation to set the boundary equation.

$$V_{ADC,min} \times K_{SNS} / I_{LOAD,min} \leq R_{SNS} \leq (V_{SNSFH} - V_{HR}) \times K_{SNS} / I_{LOAD,max} \quad (1)$$

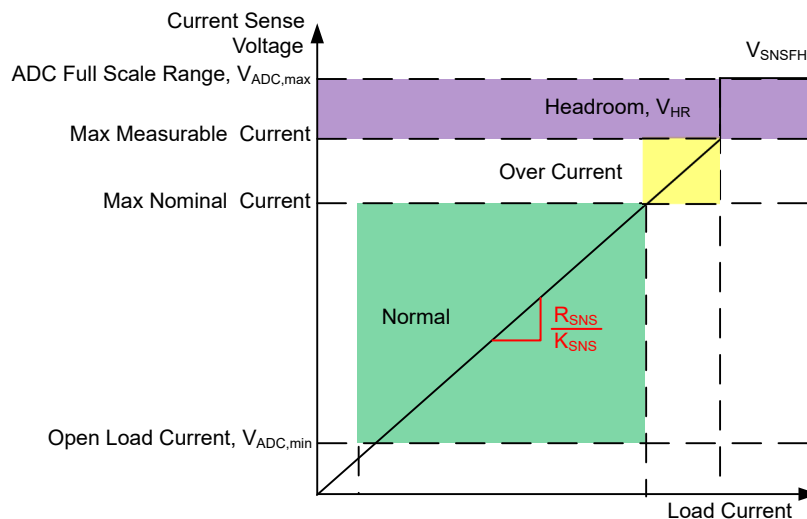


Figure 7-7. Voltage Indication on the Current-Sense Pin

The maximum current the system wants to read, $I_{LOAD,max}$, must be less than the current-limit threshold because after the current-limit threshold is tripped, the V_{SNS} value goes to V_{SNSFH} .

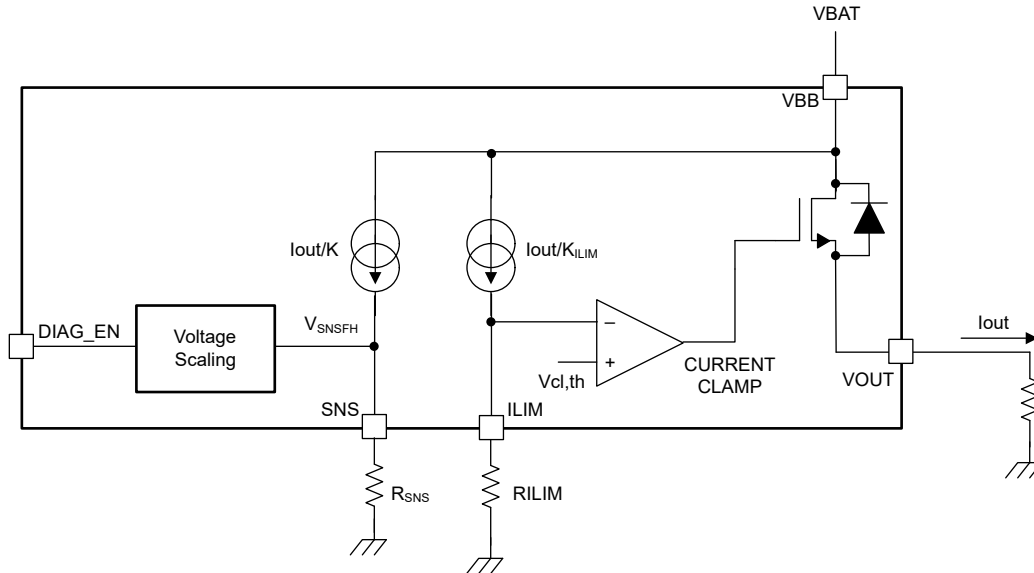


Figure 7-8. Current-Sense and Current-Limit Block Diagram

Because this scheme adapts based on the voltage coming in from the MCU, there is no need to have a Zener diode on the SNS pin to protect from high voltages.

Without any filter on SNS pin, the response of the sense clamping exhibits a slight delay (less than 10µs), resulting in a brief overshoot (less than 7V) before limiting the sense output voltage. This overshoot is not a reliability concern for the device.

7.3.4 Adjustable Current Limit

A high-accuracy adjustable current limit allows higher reliability, which protects the power supply and wires during short circuit or power up by being programmed to an acceptable level. Also, current limiting help save system costs by reducing PCB traces, connector size, capacity of the preceding power stage and possibly reducing wire gauge.

Current limit offers protection from over-stressing to the load and integrated power FET. The current limit regulates the output current to the set value, asserts the FLT pin, and pulls up the SNS pin to V_{SNSFH} if the device is set up to output that channel on the SNS pin.

The device can be programmed to different current limit values through an external resistor on the ILIM pin. There are 10 current limit settings which can be set based on resistors values in [Current Limit Setting Through External Resistor](#). Consider resistor tolerance and aging to confirm that the selected resistor value falls within the allowed range of resistor values.

Table 7-1. Current Limit Setting Through External Resistor

ALLOWED RANGE OF RESISTOR VALUES ⁽¹⁾	ILIM THRESHOLD
54.9kΩ to 60.4kΩ	250mA
41.2kΩ to 45.3kΩ	500mA
30.1kΩ to 32.4kΩ	750mA
22.1kΩ to 24.3kΩ	1A
15.8kΩ to 16.9kΩ	1.21A
9.31kΩ to 10.2kΩ	1.44A
4.64kΩ to 5.11kΩ	1.68A
2.37kΩ to 2.61kΩ	1.9A
Short to GND (< 1.1kΩ)	2.2A

Table 7-1. Current Limit Setting Through External Resistor (continued)

ALLOWED RANGE OF RESISTOR VALUES ⁽¹⁾	ILIM THRESHOLD
Open (> 87kΩ)	4.7A

(1) Interpret any resistor settings that are not listed in this table as not recommended configurations.

To set a different inrush current limit and steady state current limit, the current limit resistor can change dynamically when the device is on. Adopt the MOSFET-based control scheme to change the current limit unpremeditatedly. However, carefully consider the components and the layout at ILIM pin to minimize the capacitance at the pin. Maximum allowable external capacitance value on the ILIM pin 100pF. Higher capacitance at ILIM pin might affect the transition speed from one resistor to another, which in turn can lead to unwanted shutdown if ILIM transition and current limit fault occur simultaneously. Select a MOSFET with low input capacitance for the dynamic current limit.

A current limit event occurs when I_{OUTx} reaches the regulation threshold level, I_{CL} . When I_{OUT} reaches the current limit threshold, I_{CL} , the device can remain enabled and limit I_{OUTx} to I_{CL} . When the device remains enabled (and limits I_{OUT}), thermal shutdown can be triggered due to the high amount of power dissipation in the FET. The regulation loop response when the device is enabled into a short circuit is shown in [Enable Into Short Current Limit \(Auto-Retry Version\)](#). The figure is showing the scenario with the auto-retry version listed in [Device Comparison Table](#). The LATCH version latches off after the first thermal shutdown. Please note that the current can peak at a higher value (I_{CL_ENPS}) than the regulation threshold (I_{CL}).

When an overcurrent event occurs, the current limit must respond quickly to limit the peak current seen on short circuits (both hot and enabling into a short). Limit the peak so that the supply does not droop for a given amount of supply capacitance. This peak limiting is especially important in applications where the device is powered from a DC/DC instead of car battery.

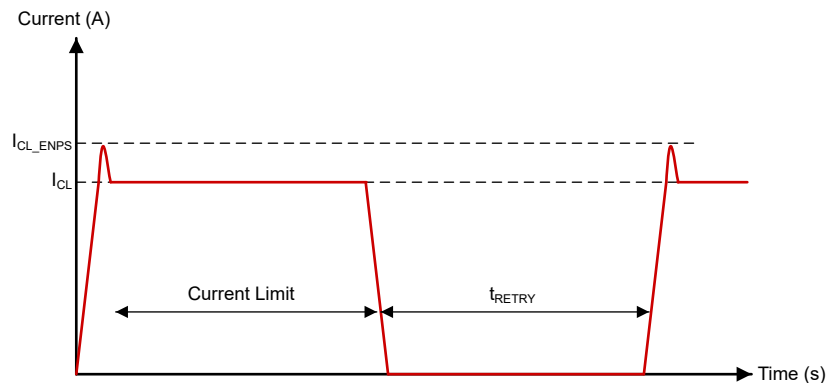


Figure 7-9. Enable Into Short Current Limit (Auto-Retry Version)

However, a higher (I_{CL_LINPK}) output current than the current limit regulation loop threshold (I_{CL}) can be available from the switch during an overload condition before the current limitation is applied.

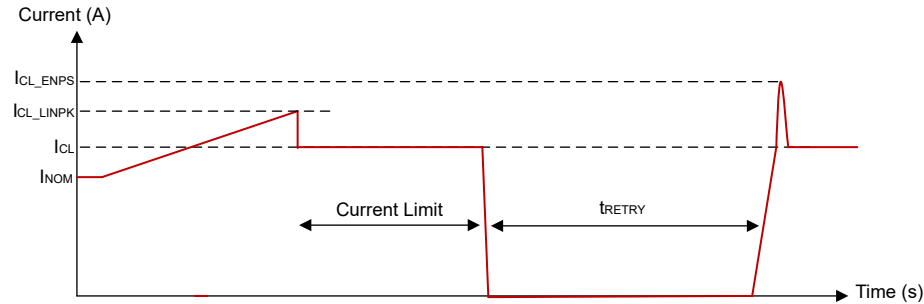


Figure 7-10. Linear Peak From Soft Short (Auto-Retry Version)

The device applies a strong pulldown to limit the current during the short circuit event while the switch is enabled. The current then drops down to zero before the current limit regulation loop engages the switch turn-on, and the behavior is similar to the enable into a short circuit case.

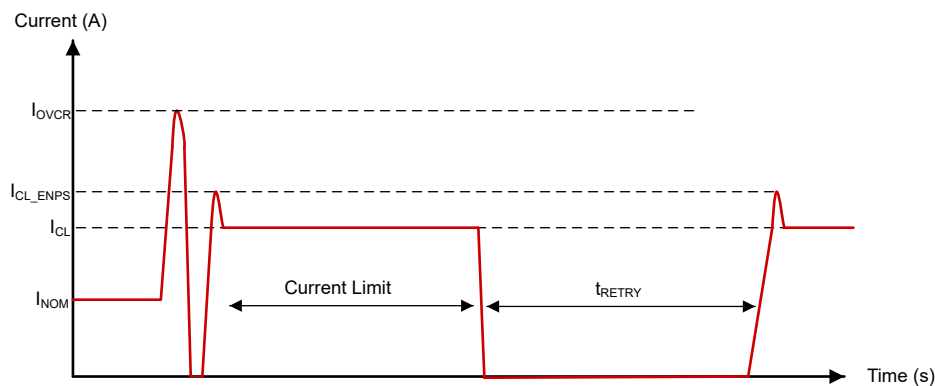


Figure 7-11. Hot Short Event (Auto-Retry Version)

For any load inductance, the reaction time for hot short turn-off is specified by the t_{OVCR} parameter. The I_{OVCR} can be estimated by $(1.6 \times I_{CL} + V_{BB} \times t_{OVCR}/L)$.

The peak current observed during hot short events depends on the timing of when a hot short is applied externally. If the hot short is applied during switch-off phase or immediately after activation via EN input, the peak current can be higher. This is because during turning ON or OFF, the internal FET is in saturation region for some time - which leads to additional peak current. The additional peak current during hot short does not pose any reliability concerns for the device.

7.3.5 Inductive-Load Switching-Off Clamp

When switching an inductive load off, the inductive reactance tends to pull the output voltage negative. Excessive negative voltage can cause the power FET to break down. To protect the power FET, an internal clamp between drain and source is implemented, namely $V_{DS(clamp)}$.

$$V_{DS(clamp)} = V_{VS} - V_{OUT} \quad (2)$$

During the period of demagnetization (t_{decay}), the power FET is turned on for inductance-energy dissipation. The total energy is dissipated in the high-side switch. Total energy includes the energy of the power supply ($E_{(VS)}$) and the energy of the load ($E_{(load)}$). If resistance is in series with inductance, some of the load energy is dissipated on the resistance.

$$E_{(HSS)} = E_{(VS)} + E_{(load)} = E_{(VS)} + E_{(L)} - E_{(R)} \quad (3)$$

When an inductive load switches off, $E_{(HSS)}$ causes high thermal stressing on the device. The upper limit of the power dissipation depends on the device intrinsic capacity, ambient temperature, and board dissipation condition.

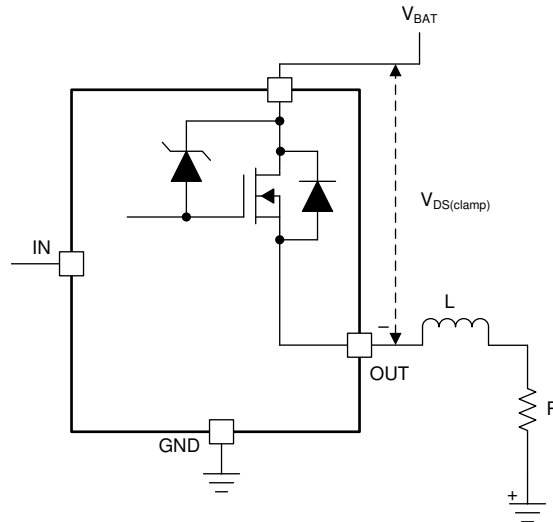


Figure 7-12. Drain-to-Source Clamping Structure

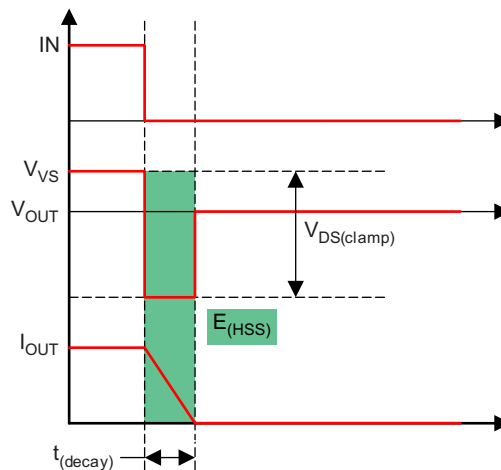


Figure 7-13. Inductive Load Switching-Off Diagram

From the perspective of the high-side switch, $E_{(HSS)}$ equals the integration value during the demagnetization period.

$$E_{(HSS)} = \int_0^{t_{(decay)}} V_{DS(clamp)} \times I_{OUT}(t) dt$$

$$t_{(decay)} = \frac{L}{R} \times \ln \left[\frac{R \times I_{OUT(max)} + |V_{OUT}|}{|V_{OUT}|} \right] \quad (4)$$

$$E_{(HSS)} = L \times \frac{V_{VS} + |V_{OUT}|}{R^2} \times \left[R \times I_{OUT(max)} - |V_{OUT}| \ln \left(\frac{R \times I_{OUT(max)} + |V_{OUT}|}{|V_{OUT}|} \right) \right]$$

When R approximately equals 0, $E_{(HSD)}$ can be given simply as:

$$E_{(HSS)} = \frac{1}{2} \times L \times I_{OUT(max)}^2 \frac{V_{VS} + |V_{OUT}|}{|V_{OUT}|} \quad (5)$$

$V_{DS(clamp)}$ voltage changes by approximately 1V during the active-to-standby transition after switching off an inductive load. This change in clamp voltage does not present any risk to the long-term reliability of the device.

The recommendation for PWM-controlled inductive loads is to add the external freewheeling circuitry shown in Figure 7-14 to protect the device from repetitive power stressing. TVS is used to achieve the fast decay.

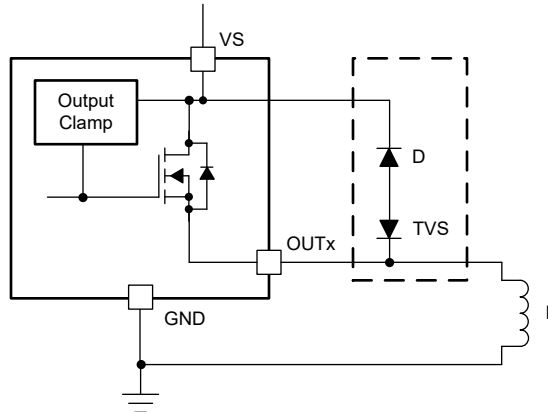


Figure 7-14. Protection With External Circuitry

7.3.6 Fault Detection and Reporting

7.3.6.1 Diagnostic Enable Function

The DIAG_EN pin enables or disables the diagnostic functions. If multiple devices are used, but the ADC resource is limited in the microcontroller, the MCU can use GPIOs to set DIAG_EN high to enable the diagnostics of one device while disabling the diagnostics of the other devices by setting DIAG_EN low. In addition, the device can keep the power consumption to a minimum by setting DIAG_EN and ENx low.

7.3.6.2 Multiplexing of Current Sense

SEL pin is used to multiplex the shared current-sense function among the two channels within the same device. Pulling the pin high or low sets the corresponding channel to be output on the SNS pin if DIAG_EN is high. FLT represents a global interrupt that goes low if a fault occurs on any channel, except for open load and short-to-battery faults. For open load and short-to-battery faults, FLT goes low only if the selected channel has the fault.

If current sense information is multiplexed across different devices, do not directly tie the SNS pins together across multiple devices. When the DIAG_EN is LOW, there is an internal clamp at SNS pin that clamps the voltage to approximately 2V. One device SNS pin can affect the SNS readback of other devices if tied directly.

To use the SNS pin across multiple devices, connect individual SNS pin to different analog input pins of MCU, as illustrated in Figure 7-15. Alternatively, an external analog MUX can be used to connect to one MCU pin, as illustrated in Figure 7-16.

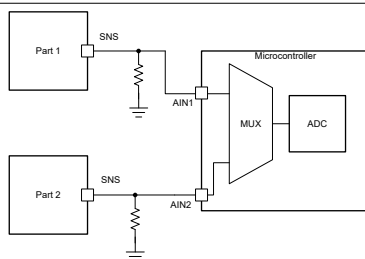


Figure 7-15. SNS Sharing Across Multiple Devices
Method 1

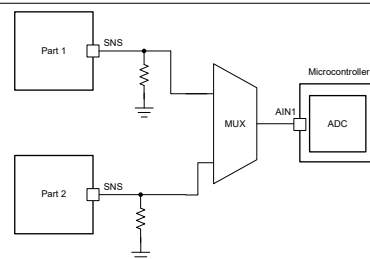


Figure 7-16. SNS Sharing Across Multiple Devices
Method 2

Table 7-2. Diagnosis Configuration Table

DIAG_EN	ENx	SEL	SNS ACTIVATED CHANNEL	SNS	FLT	PROTECTIONS AND DIAGNOSTICS
L	H	—	—	0V. Clamp to 2V internally if external voltage is applied to the pin.	See Fault Table	SNS disabled, FLT reporting, full protection
	L				High-Z	Diagnostics disabled, no protection
H	—	0	Channel 1	See Fault Table	See Fault Table	See Fault Table
		1	Channel 2			

7.3.6.3 FLT Reporting

The FLT pin is used to monitor the fault condition among all the channels. When a fault condition (except open load and short-to-battery faults) occurs on any channel, the FLT pin is pulled down to GND. A 3.3V or 5V external pullup is required to match the supply level of the microcontroller. The FLT pin reports faults as long as the device is not in the SLEEP or LOW POWER MODE. For open load and short-to-battery faults, FLT goes low only if the selected channel has the fault.

After the FLT report, the microcontroller can check and identify the channel in fault status by multiplexed current sensing. The SNS pin also works as a fault report with an internal pullup voltage, V_{SNSFH} if DIAG_EN is high.

7.3.6.4 Fault Table

Table 7-3. Fault Table

CONDITIONS	ENx	OUTx	SNS (If DIAG_EN is high)	FLT (with external pull-up)	BEHAVIOR	FAULT RECOVERY
Normal	L	L	0	H	Normal	—
	H	$V_{BB} - I_{LOAD} \times R_{ON}$	I_{LOAD} / K_{SNS}	H	Normal	—
Overcurrent	H	$V_{BB} - I_{LIM} \times R_{ON}$	V_{SNSFH}	L	Holds the current at the current limit until thermal shutdown or when the overcurrent event is removed.	Auto
Open load, Short to battery	L	H	V_{SNSFH}	L	Internal pull-up resistor is active. Fault is asserted when $V_{VS} - V_{OUTx} < V_{(ol,off)}$	Auto
	H	H	I_{LOAD} / K_{SNS}	H	Normal behavior. User can make judgment based on SNS pin output.	—
Hot short	H	L	V_{SNSFH}	L	Device will immediately shutdown, and re-enable into current limit.	Auto-retry into current limit until thermal shutdown. Auto-retry version repeats until the fault goes away. Latch version needs toggle EN after first thermal shutdown.
Enable into permanent short	L → H	L	V_{SNSFH}	L	Device enables into current limit until thermal shutdown.	Enable into current limit until thermal shutdown. Auto-retry version will repeat until the fault goes away. Latch version will need toggle EN after first thermal shutdown.

Table 7-3. Fault Table (continued)

CONDITIONS	ENx	OUTx	SNS (if DIAG_EN is high)	FLT (with external pull-up)	BEHAVIOR	FAULT RECOVERY
Absolute thermal shutdown, Relative thermal shutdown	H	L	V_{SNSFH}	L	Shuts down when devices hits relative or absolute thermal shutdown.	For auto-retry version, output auto-retry after t_{RETRY} . Fault recovers when $T_J < T_{HYS}$ or when ENx toggles. Latch version can recover only when EN toggles.
Reverse polarity	X	X	X		X	Channel turns on to lower power dissipation. Current into ground pin must be limited by external ground network.

7.3.7 Full Diagnostics

7.3.7.1 Short-to-GND and Overload Detection

When a channel is on, a short to GND or overload condition causes overcurrent. If the overcurrent triggers either the internal or external current-limit threshold, the fault condition is reported out. The microcontroller can handle the overcurrent by turning off the switch. The device clamps the current to I_{CL} until thermal shutdown. The auto-retry version automatically recovers when the fault condition is removed.

In a hot short condition, when the short-circuit is applied when the EN is HIGH, the device shuts down immediately and auto-retry the same as enable into permanent short condition, as shown in [Hot Short Event \(Auto-Retry Version\)](#).

7.3.7.2 Open-Load Detection

7.3.7.2.1 Channel On

When a channel is ON, benefiting from the high-accuracy current sense in the small current range, an open-load event can be detected as an ultra-low V_{SNS} and handled by the microcontroller. Note that the detection is not reported on the $\overline{FLT}$ pin or the fault registers. The microcontroller must toggle the SEL pin to output the correct channel out on the SNS pin.

7.3.7.2.2 Channel Off

In the OFF state, when DIAG_EN is high, there is an internal pull-up resistor R_{PU} that pulls up a channel to V_{BB} . The specific channel that gets pulled up is based on the SEL pin, and the other channels do not have the pull-up resistor engaged.

If there is load present at the selected channel, then the output voltage is pulled to around 0V, as the load is much stronger than the R_{PU} . In the case of an open load, the output voltage is pulled close to the supply voltage by the R_{PU} . If $V_{BB} - V_{OUT} < V_{OL,off}$ for the selected channel, the $\overline{FLT}$ pin goes low to indicate the fault to the MCU, and the SNS pin is pulled up to I_{SNSFH} .

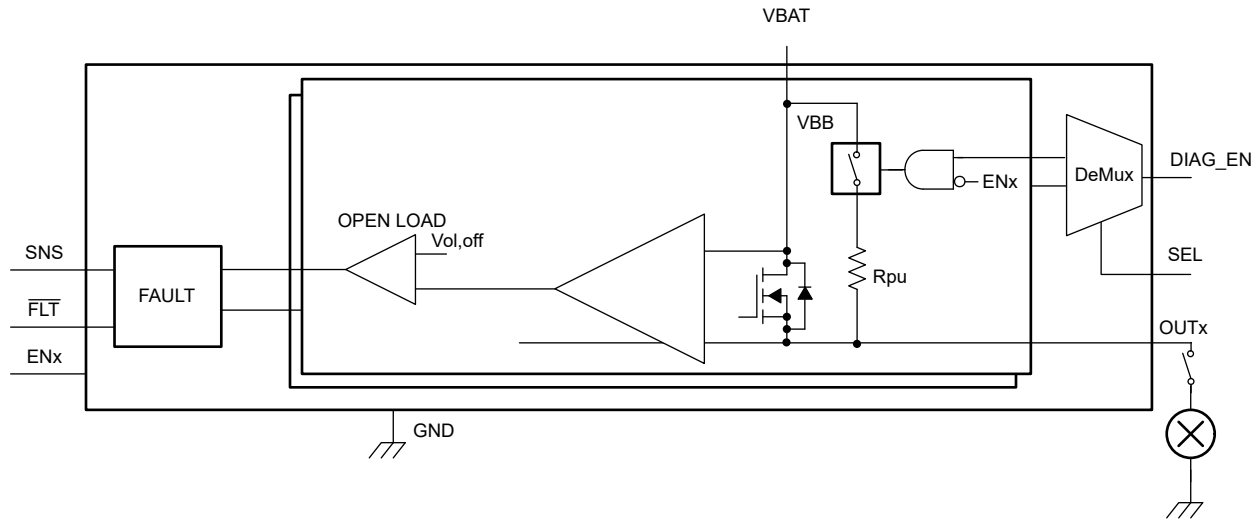


Figure 7-17. Open-Load Detection in Off-State

The value of the internal pull-up resistor (R_{PU}) can cause LED loads to flicker during the OFF state (when DIAG_EN in high). External pull-down resistors on the output channels and switchable pull-up resistor network resolves the observed flicker.

If the time constant due the R_{PU} and output capacitor is too large for normal diagnosis timing, the DIAG_EN must be toggled longer for proper open-load detection.

7.3.7.3 Short-to-Battery Detection

Short-to-battery has the same detection mechanism and behavior as open-load detection, in both the on-state and off-state. See [Fault Table](#) for more details.

7.3.7.4 Reverse-Polarity and Battery Protection

Reverse-polarity, commonly referred to as reverse battery, occurs when the ground of the device goes to the battery potential, $V_{GND} = V_{BAT}$, and the supply pin goes to ground, $V_{BB} = 0V$. In this case, if the EN1 pin has a path to the *ground* plane, then the FET turns on to lower the power dissipation through the main channel and prevent current flow through the body diode. Note that the resistor/diode ground network (if there is not a central blocking diode on the supply) must be present for the device to protect the device during a reverse battery event.

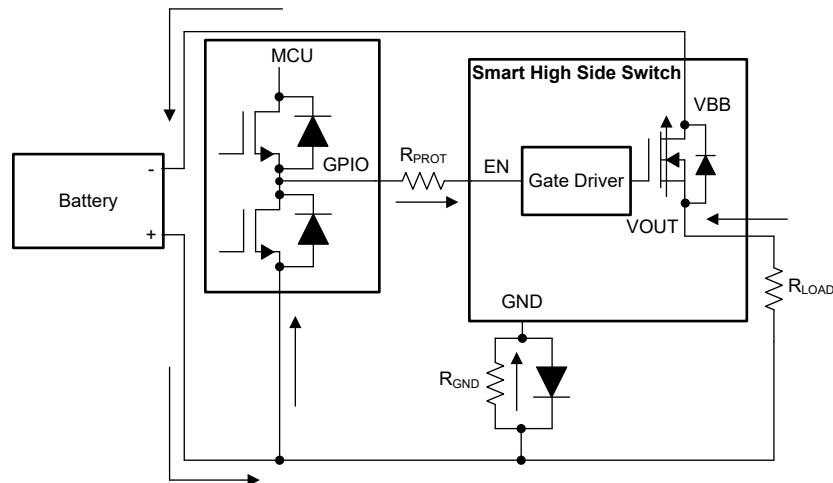


Figure 7-18. Reverse Battery Circuit

For more external protection circuitry information, see [Reverse Battery Protection](#). See the fault truth table in [Fault Table](#) for more details.

7.3.7.5 Thermal Fault Detection

To protect the device in severe power stressing cases, the device implements two types of thermal fault detection, absolute temperature protection (absolute thermal shutdown) and dynamic temperature protection (relative thermal shutdown). Respective temperature sensors are integrated close to each power FET, so the thermal fault is reported by each channel. This arrangement can help the device keep the cross-channel effect to a minimum when some channels are in a thermal fault condition.

7.3.7.5.1 Thermal Protection Behavior

The thermal protection behavior can be split up into two categories of events that can occur. [Thermal Behavior for Auto-Retry Version](#) shows each of these categories.

1. **Relative thermal shutdown:** the device is enabled into an overcurrent event. The output current rises up to the I_{ILIM} level and the $\overline{FLT}$ goes low. With this large amount of current going through the junction temperature of the FET increases rapidly with respect to the controller temperature. When the power FET temperature rises T_{REL} amount above the controller junction temperature $\Delta T = T_{FET} - T_{CON} > T_{REL}$, the device shuts down. For auto-retry version, after t_{RETRY} , the part tries to restart itself. Latch version requires EN to be toggled to re-enable the channel. The $\overline{FLT}$ is asserted until the fault condition is cleared.
2. **Absolute thermal shutdown:** The device is still enabled in an overcurrent event. However, in this case the junction temperature rises up and hits an absolute reference temperature, T_{ABS} , and then shuts down. For auto-retry version, the device does not recover until both $T_J < T_{ABS} - T_{hys}$ and the t_{RETRY} timer has expired. For latch version, toggling EN is required to re-enable the channel.

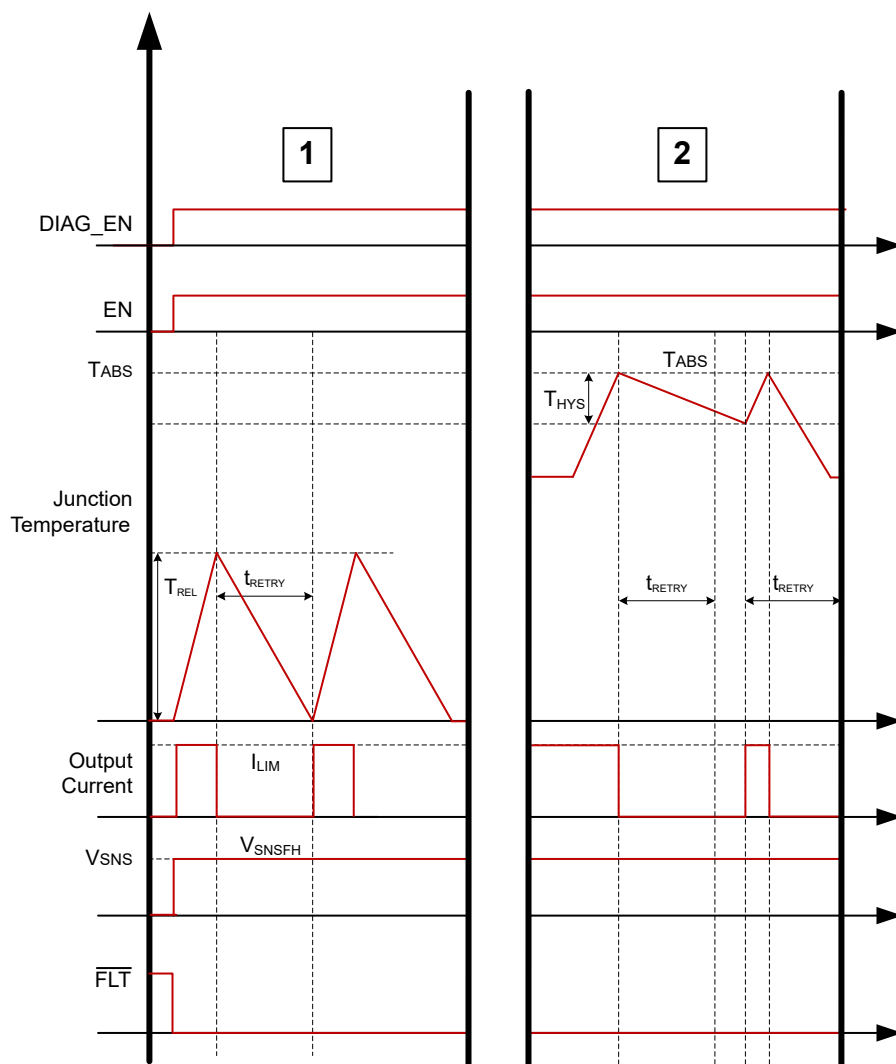


Figure 7-19. Thermal Behavior for Auto-Retry Version

7.3.8 Full Protections

7.3.8.1 UVLO Protection

The device monitors the supply voltage V_{VBB} , to prevent unpredicted behaviors when V_{VBB} is too low. When V_{VBB} falls down to V_{UVLOF} , the device shuts down. When V_{VBB} rises up to V_{UVLOR} , the device turns on.

7.3.8.2 Loss of GND Protection

When loss of GND occurs, output is turned off regardless of whether the input signal is high or low, and the part is not powered.

Case 1 (loss of device/IC GND): loss of GND protection is active when the thermal pad (Tab), IC GND, and current limit ground are one trace connected to the system ground, as shown in [Figure 7-20](#).

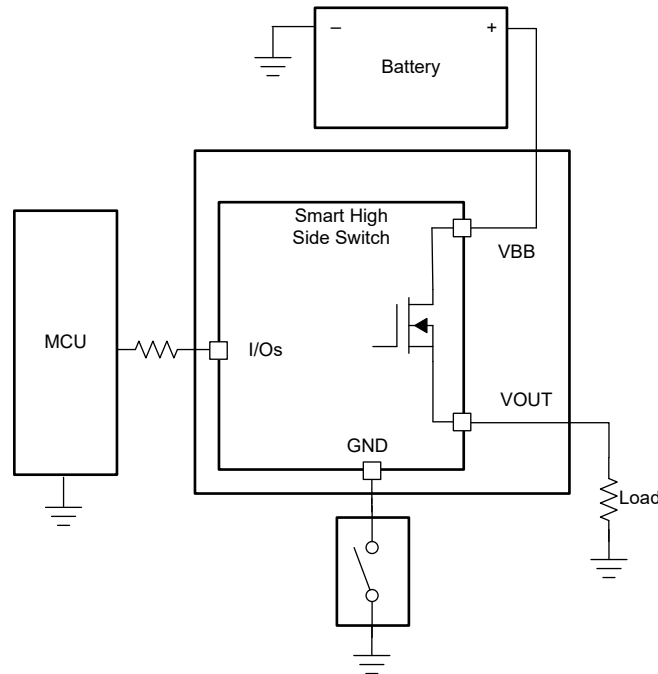


Figure 7-20. Loss of Device GND

Case 2 (loss of module GND): when the whole ECU module GND is lost, protections are also active. At this condition, the load GND remains connected.

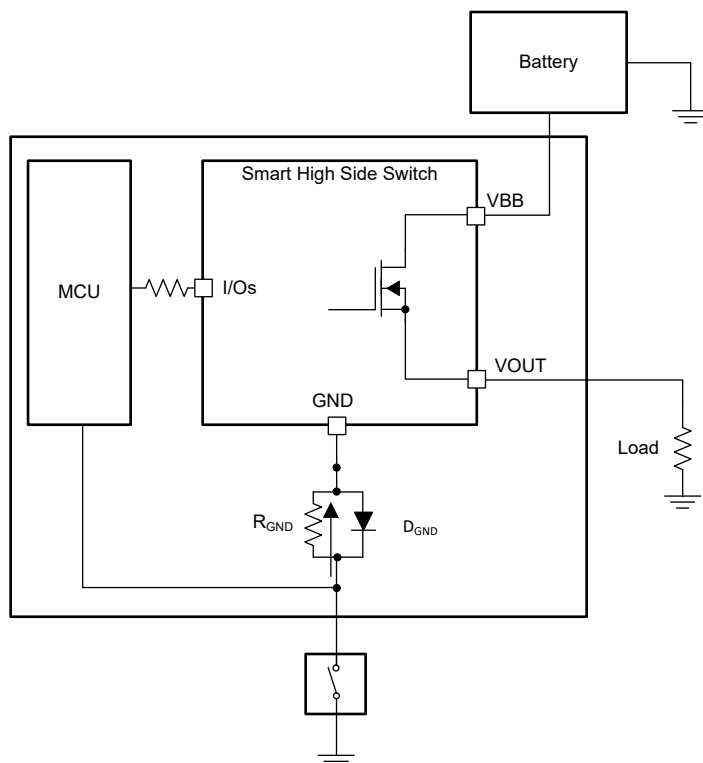


Figure 7-21. Loss of Module GND

7.3.8.3 Loss of Power Supply Protection

When loss of supply occurs, output is turned off regardless of whether the input is high or low. For a resistive or capacitive load, loss of supply protection is easy to achieve due to no more power. The worst case is a charged inductive load. In this case, the current is driven from all of the IOs to maintain the inductance output loop. TI recommends either the MCU serial resistor plus the GND network (diode and resistor in parallel) or external free-wheeling circuitry.

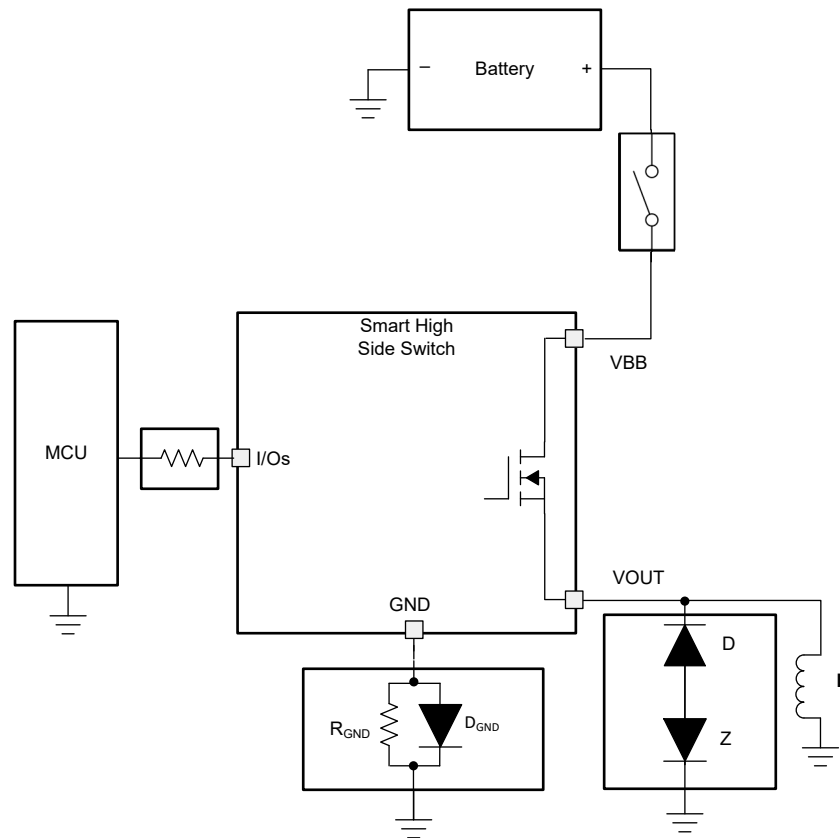


Figure 7-22. Loss of Battery

7.3.8.4 Reverse Battery Protection

Method 1: Block diode connected with V_{BB} . Both the device and load are protected when in reverse polarity. The blocking diode does not allow any of the current to flow during reverse battery condition.

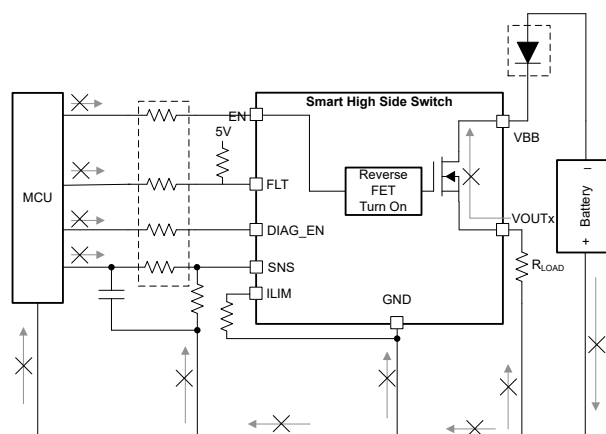


Figure 7-23. Reverse Protection With Block Diode

Method 2 (GND network protection): Only the high-side device is protected under this connection. The load reverse current is limited by the impedance of the load. When reverse polarity occurs, the continuous reverse current through the power FET must not make the heat build up be greater than the absolute maximum junction temperature. Device temperature can be calculated using the $R_{ON(REV)}$ value and the $R_{\theta JA}$ specification. In the reverse battery condition, confirm that the FET comes on to lower the power dissipation. This action is achieved through the path from EN to system ground where the positive voltage is being applied. No matter what types of connection are between the device GND and the board GND, if a GND voltage shift occurs, confirm the following proper connections for the normal operation:

- Connect the current limit programmable resistor to the device GND.

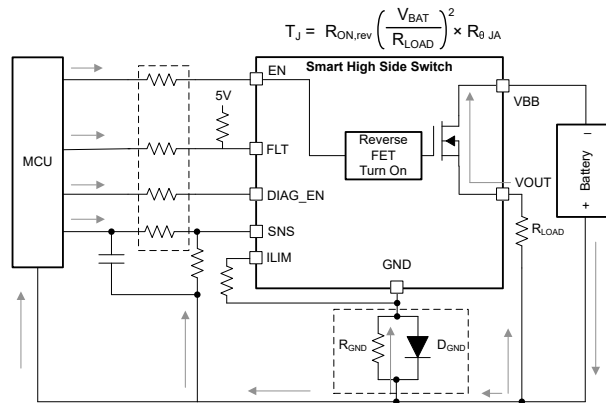


Figure 7-24. Reverse Protection With GND Network

- **Recommendation – resistor and diode in parallel:** A peak negative spike can occur when the inductive load is switching off, which can damage the HSD or the diode. So, TI recommends a resistor in parallel with the diode when driving an inductive load. The recommended selection are a 4.7kΩ resistor in parallel with an $I_F > 100\text{mA}$ diode. If multiple high-side switches are used, the resistor and diode can be shared among devices.
- **Ground Resistor:** The higher resistor value contributes to a better current limit effect when the reverse battery or negative ISO pulses.

$$R_{GND} \geq \frac{(-V_{CC})}{(-I_{GND})} \quad (6)$$

where

- $-V_{CC}$ is the maximum reverse battery voltage (typically -16V).
- $-I_{GND}$ is the maximum reverse current the ground pin can withstand, which is available in the [Absolute Maximum Ratings](#).
- **Ground Diode:** A diode is needed to block the reverse voltage, which also brings a ground shift ($\approx 600\text{mV}$). Additionally, the diode must be $\approx 200\text{V}$ reverse voltage for the ISO 7637 pulse 1 testing so that it does not get biased.

7.3.8.5 Protection for MCU I/Os

In many conditions, such as the negative ISO pulse, or the loss of battery with an inductive load, a negative potential on the device GND pin can damage the MCU I/O pins (more likely, the internal circuitry connected to the pins). Therefore, the serial resistors between MCU and HSS are required.

Also, for proper protection against loss of GND, TI recommends 10kΩ resistance for the R_{PROT} resistors.

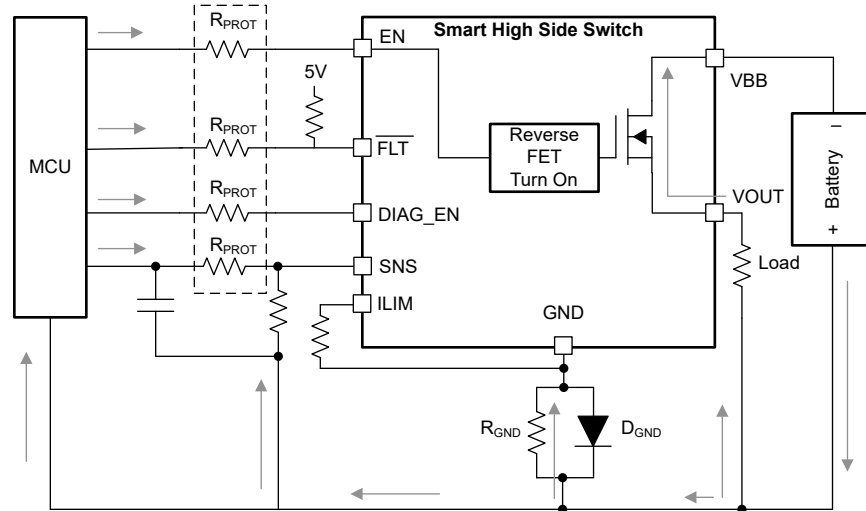


Figure 7-25. MCU I/O Protections

7.4 Device Functional Modes

7.4.1 Working Modes

This device has several states to transition into based on the ENx pins, DIAG_EN pin and load conditions.

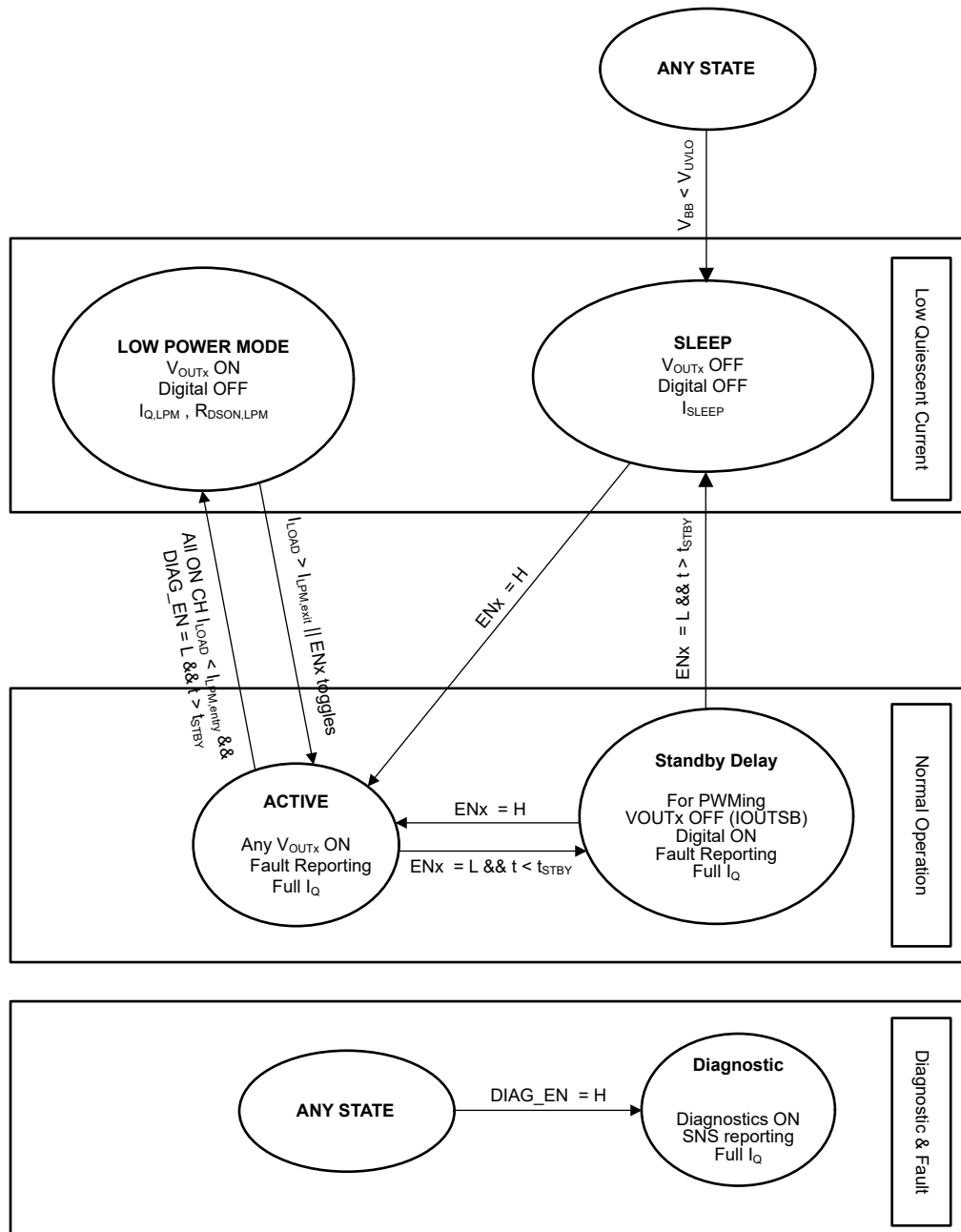


Figure 7-26. State Diagram

7.4.1.1 SLEEP

In the SLEEP state, everything inside the device is turned off and the quiescent current is the I_{SLEEP} . The device only transitions out of the SLEEP state if the ENx pins or $DIAG_EN$ pin is pulled high. From the SLEEP state, the device can transfer into the ACTIVE state if any of the ENx pins are pulled high, or into the DIAGNOSTIC state if the $DIAG_EN$ pin, without any of the ENx pins, goes high. During these transitions, the current consumption exceeds the specification for approximately $6\mu s$ due to the internal charge pump, oscillator and digital circuit blocks turning on.

Additionally, if the device is in any of the states and V_{BB} drops to less than V_{UVLOF} , the device transitions into SLEEP state.

7.4.1.2 DIAGNOSTIC

The DIAGNOSTIC state is when the device is outputting diagnostics on the SNS and $\overline{\text{FLT}}$ pins. This state occurs when the device is in any previous state and the DIAG_EN pin goes high. The off-state diagnostics are comprised of open load detection in off-state and short-to-battery detection. The SNS pin only outputs a fault for the channel associated to the SEL pin value. From the DIAGNOSTIC state, the device transfers into the ACTIVE state if the DIAG_EN pin goes back low and any channel is on, or into the STANDBY DELAY state if all channels are off.

7.4.1.3 ACTIVE

The ACTIVE state is when any of the channel outputs are on by the ENx pin associated. In the ACTIVE state, the current limit value is set by the external resistor on the ILIM pin. If the DIAG_EN pin is pulled high while in the ACTIVE state, the SNS pin outputs a proportional current to the load current of the channel associated to the SEL pin configuration until a fault occurs on that channel. The device can transition out of the ACTIVE state by turning off all of the channels while DIAG_EN is high or low, or a fault occurring. If all of the channels turn off and DIAG_EN is high, the device transitions into the DIAGNOSTIC state. If all of the channels turn off and the DIAG_EN pin is low, then the device transfers into the STANDBY DELAY state.

7.4.1.4 STANDBY DELAY

The STANDBY DELAY state is when the ENx pins are all low, the outputs are all turned off, and the DIAG_EN pin is also low, but there has not yet been t_{STBY} amount of time. This state is included so that the channel outputs are able to support PWM without all of the internal rails being cut off and put into SLEEP mode. Output leakage current per channel is approximately 3 μA (typical) during the STANDBY DELAY state.

After the device has waited t_{STBY} , the device completely shuts down and transitions into SLEEP. However, if during t_{STBY} , ENx goes high, the device transitions into ACTIVE without shutting completely down. Similarly if the DIAG_EN goes high, the device transitions into DIAGNOSTIC.

7.4.1.5 LOW POWER MODE

The LOW POWER MODE state is when the channels that are active are below the $I_{\text{LPM,entry}}$ level for longer than t_{STBY} and the DIAG_EN is low. The device turns off all unnecessary internal blocks and reduces the quiescent current from I_{Q} to $I_{\text{Q,LPM}}$. The device is still protected but no diagnostics or fault reporting is possible until device comes out of this mode. For more information on Low Power Mode see [Low Power Mode](#).

8 Application and Implementation

Note

Information in the following applications sections is not part of the TI component specification, and TI does not warrant its accuracy or completeness. TI's customers are responsible for determining suitability of components for their purposes, as well as validating and testing their design implementation to confirm system functionality.

8.1 Application Information

The TPS2HC120-Q1 device is capable of driving a wide variety of resistive, inductive, and capacitive loads, including the low-wattage bulbs, LEDs, relays, solenoids, heaters, and sub-modules. Full diagnostics and high-accuracy current-sense features enable intelligent control of the load. An external adjustable current limit improves the reliability of the whole system by clamping the inrush or overload current.

8.2 EMC Transient Disturbances Test

Due to the severe electrical conditions in the automotive environment, immunity capacity against electrical transient disturbances is required, especially for a high side power switch, which connects directly to the battery. Detailed test requirements are in accordance with the ISO 7637-2:2011 and ISO 16750-2:2010 standards.

Table 8-1. ISO 7637-2:2011(E) in 12V System⁽¹⁾⁽²⁾⁽³⁾

TEST ITEM	TEST PULSE SEVERITY LEVEL AND VS ACCORDINGLY		PULSE DURATION (t _d)	MINIMUM NUMBER OF PULSES OR TEST TIME	BURST-CYCLE PULSE-REPETITION TIME		INPUT RESISTANCE (Ω)	FUNCTION PERFORMANCE STATUS CLASSIFICATION
	LEVEL	Vs/V			MIN	MAX		
1	III	–112	2ms	500 pulses	0.5s	—	10	Status II
2a	III	55	50μs	500 pulses	0.2s	5s	2	Status II
2b	IV	10	0.2s to 2s	10 pulses	0.5s	5s	0 to 0.05	Status II
3a	IV	–220	0.1μs	1h	90ms	100ms	50	Status II
3b	IV	150	0.1μs	1h	90ms	100ms	50	Status II

(1) Tested both under input low condition and high condition.

(2) GND pin network is a 1kΩ resistor in parallel with a diode BAS21-7F.

(3) Status II: The function does not perform as designed during the test, but returns automatically to normal operation after the test.

Table 8-2. ISO 16750-2:2010(E) Load Dump Test B in 12V System⁽¹⁾⁽²⁾⁽³⁾⁽⁴⁾

TEST ITEM	TEST PULSE SEVERITY LEVEL AND VS ACCORDINGLY		PULSE DURATION (t _d)	MINIMUM NUMBER OF PULSES OR TEST TIME	BURST-CYCLE PULSE-REPETITION TIME	INPUT RESISTANCE (Ω)	FUNCTION PERFORMANCE STATUS CLASSIFICATION
	LEVEL	Vs/V					
Test B	N/A	35	40ms to 400ms	5 pulses	60s	0.5 to 4	Status II

(1) Tested both under input low condition and high condition (DIAG_EN, ENx, and VBB are all classified as inputs).

(2) Considering the worst test condition, the device is tested without any filter capacitors on VBB and VOUTx.

(3) The GND pin network is a 1kΩ resistor in parallel with a diode BAS21-7F.

(4) Status II: The function does not perform as designed during the test, but returns automatically to normal operation after the test.

8.3 Typical Application

Figure 8-1 shows an example of the external circuitry connections for TPS2HC120.

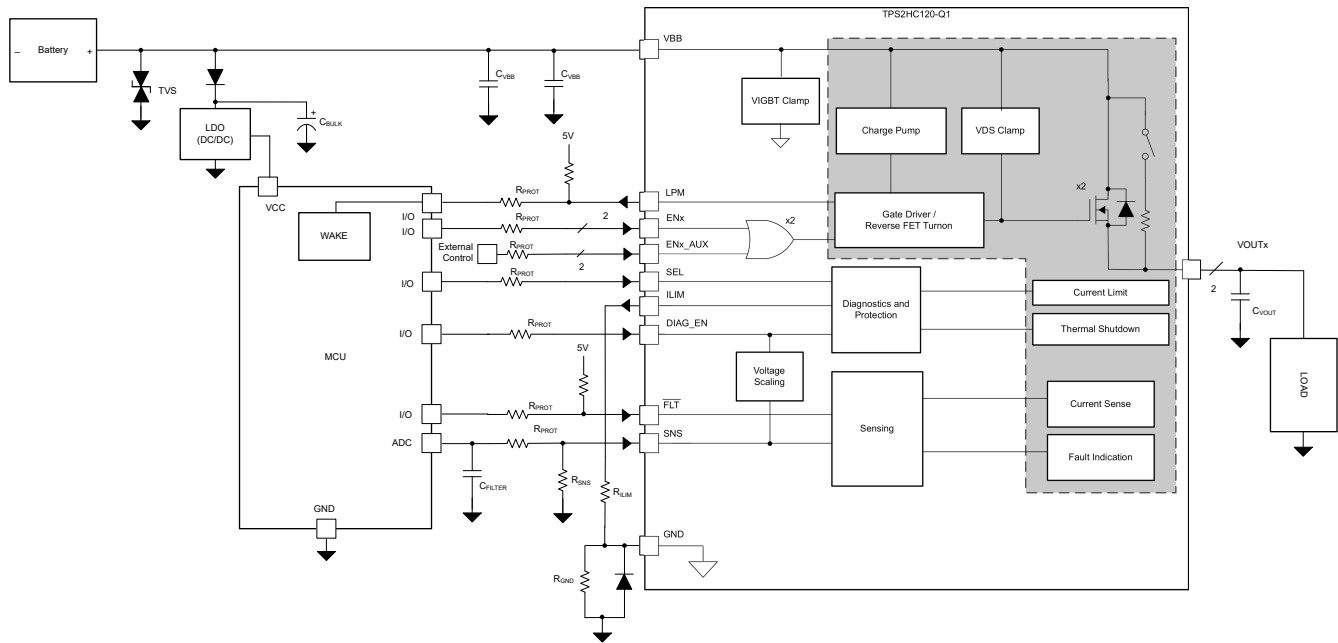


Figure 8-1. Typical Application Diagram

Table 8-3. Recommended Component Values

COMPONENT	DESCRIPTION	PURPOSE
TVS	SMBJ39CA	Filter voltage transients coming from battery (ISO7637-2)
C_{VBB}	220nF	Better EMI performance
C_{IC}	15nF	Minimal amount of capacitance on input for EMI mitigation
C_{BULK}	10 μ F	Help filter voltage transients on the supply rail
R_{PROT}	10k Ω	Protection resistor for microcontroller and device I/O pins
R_{LIM}	Discrete values as listed in Table 7-1	Set current limit threshold
R_{SNS}	1k Ω	Translate the sense current into sense voltage
C_{FILTER}	100nF	Coupled with R_{PROT} on the SNS line creates a low-pass filter to filter out noise going into the ADC of the MCU
C_{VOUT}	22nF	Improves EMI performance, filtering of voltage transients
R_{PULLUP}	5k Ω	Pull up resistor for open-drain pins ($\overline{FLT}$ and LPM)
R_{GND}	1k Ω	Stabilize GND potential during turn-off of inductive load
D_{GND}	BAS21 Diode	Keeps GND close to system ground during normal operation

8.3.1 Design Requirements

Table 8-4. Example Design Requirements

PARAMETER	VALUE
V_{DIAG_EN}	5V
$I_{LOAD,max}$	1A
$I_{LOAD,min}$	10mA
$V_{ADC,min}$	5mV
V_{HR}	1V

8.3.2 Detailed Design Procedure

To keep the 1A nominal current in the current-sense range from 0V to 4V, calculate the $R_{(SNS)}$ resistor using Equation 7. To achieve better current-sense accuracy, a 1% tolerance or better resistor is preferred.

$$V_{ADC,min} \times K_{SNS} / I_{LOAD,min} \leq R_{SNS} \leq (V_{SNSFH} - V_{HR}) \times K_{SNS} / I_{LOAD,max} \quad (7)$$

The design requirement listed in Table 8-4 yields $520\Omega \leq R_{SNS} \leq 4160\Omega$, and $1k\Omega$ R_{SNS} satisfies the requirements.

To set the adjustable current limit value, use the $R_{(ILIM)}$ recommended in the Table 7-1. In this application, to leave enough margin for the current transient and ripple, a $9.76k\Omega$ R_{ILIM} resistor satisfies the requirements.

8.3.3 Application Curves

Figure 8-2 shows a test example of soft-start when driving a big capacitive load. Figure 8-3 shows the VDS clamp engaging during inductive load discharge.

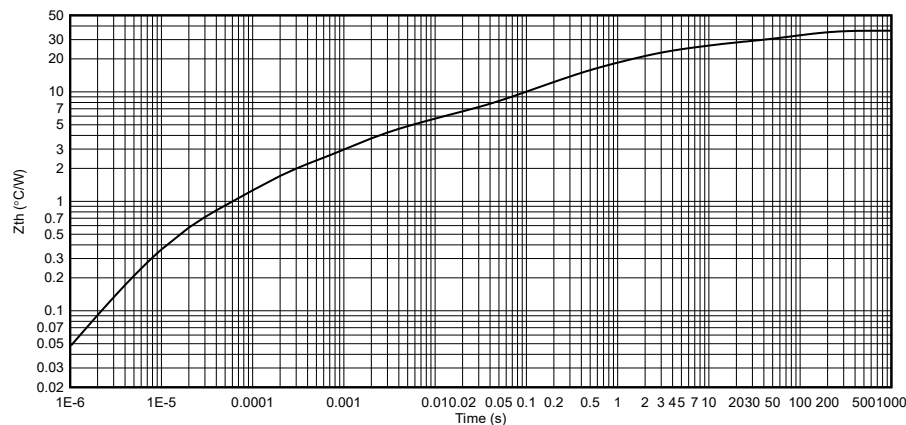
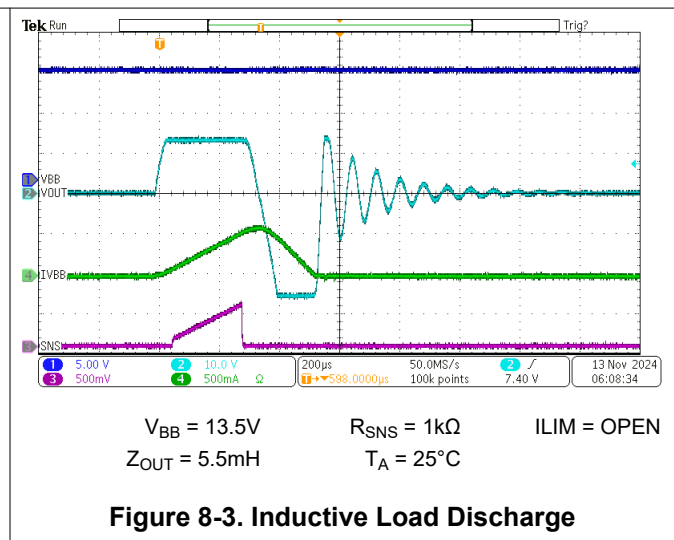
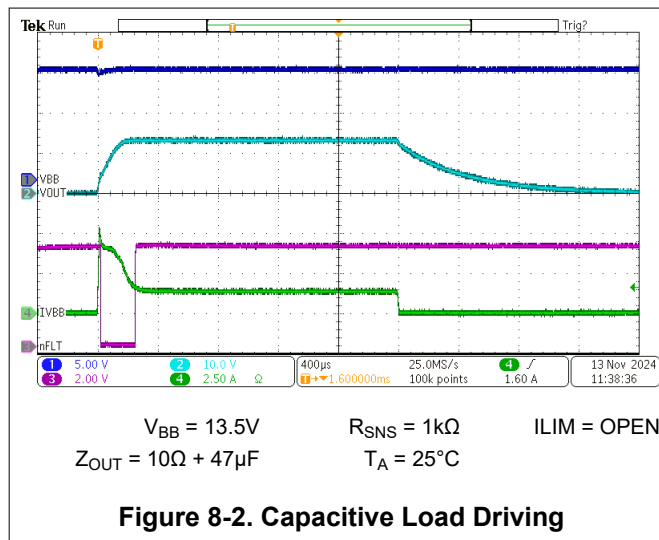


Figure 8-4. Transient Thermal Impedance (Junction to Ambient), $T_A = 105^\circ C$, JEDEC Standard 2s2p PCB Layout With Thermal Vias

8.4 Power Supply Recommendations

The device is qualified for both automotive and industrial applications. The normal power supply connection is a 12V automotive system. The supply voltage must be within the range specified in the Recommended Operating Conditions.

Table 8-5. Voltage Operating Ranges

VBB VOLTAGE RANGE	NOTE
3V to 6V	Extended lower 12V automotive battery operation such as cold crank and start-stop. Device is fully functional and protected but some parametrics such as R_{ON} , current sense accuracy, current limit accuracy and timing parameters can deviate from specifications. Check the individual specifications in Electrical Characteristics to confirm the voltage range it is applicable for. Device can not enter Low Power Mode in this voltage range.
6V to 18V	Nominal 12V automotive battery voltage range. All parametric specifications apply and the device is fully functional and protected.
18V to 24V	Extended upper 12V automotive battery operation such as double battery. Device is fully functional and protected but some parametrics such as R_{ON} , current sense accuracy, current limit accuracy, and timing parameters can deviate from specifications. Check the individual specifications in Electrical Characteristics to confirm the voltage range it is applicable for.
35V	Load dump voltage. Device is operational and lets the pulse pass through without being damaged but does not protect against short circuits.

8.5 Layout

8.5.1 Layout Guidelines

To prevent thermal shutdown, T_J must be less than 150°C. The HTSSOP package has good thermal impedance. However, the PCB layout is very important. Good PCB design can optimize heat transfer, which is absolutely essential for the long-term reliability of the device.

- Maximize the copper coverage on the PCB to increase the thermal conductivity of the board. The major heat flow path from the package to the ambient is through the copper on the PCB. Maximum copper is extremely important when there are not any heat sinks attached to the PCB on the other side of the package.
- Add as many thermal vias as possible directly under the package ground pad to optimize the thermal conductivity of the board.
- All thermal vias must either be plated shut or plugged and capped on both sides of the board to prevent solder voids. To confirm reliability and performance, the solder coverage must be at least 85%.

8.5.2 Layout Examples

8.5.2.1 Without a GND Network

Without a GND network, tie the thermal pad directly to the board GND copper for better thermal performance.

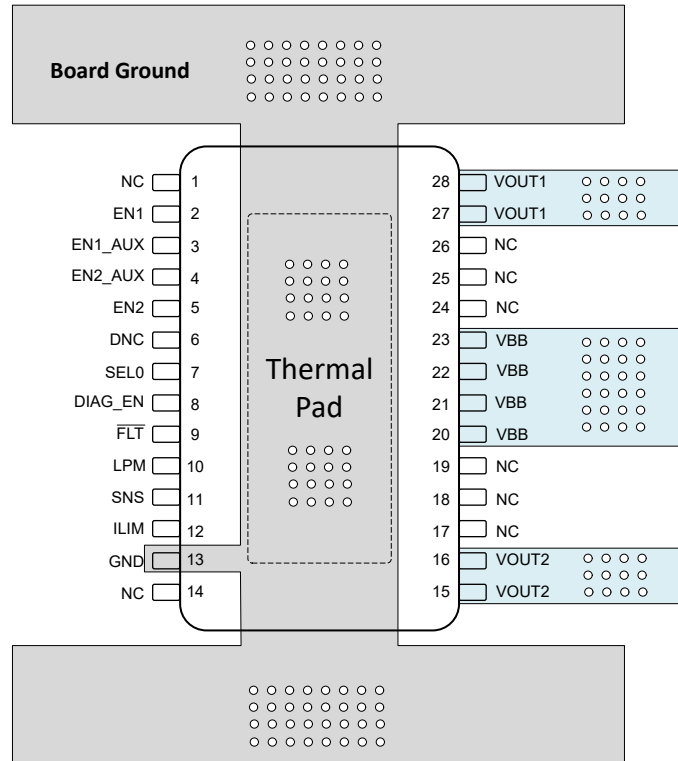


Figure 8-5. Layout Example Without a GND Network

8.5.2.2 With a GND Network

With a GND network, tie the thermal pad with a single trace through the GND network to the board GND copper. Have more IC GND coverage to get better thermal performance of the part.

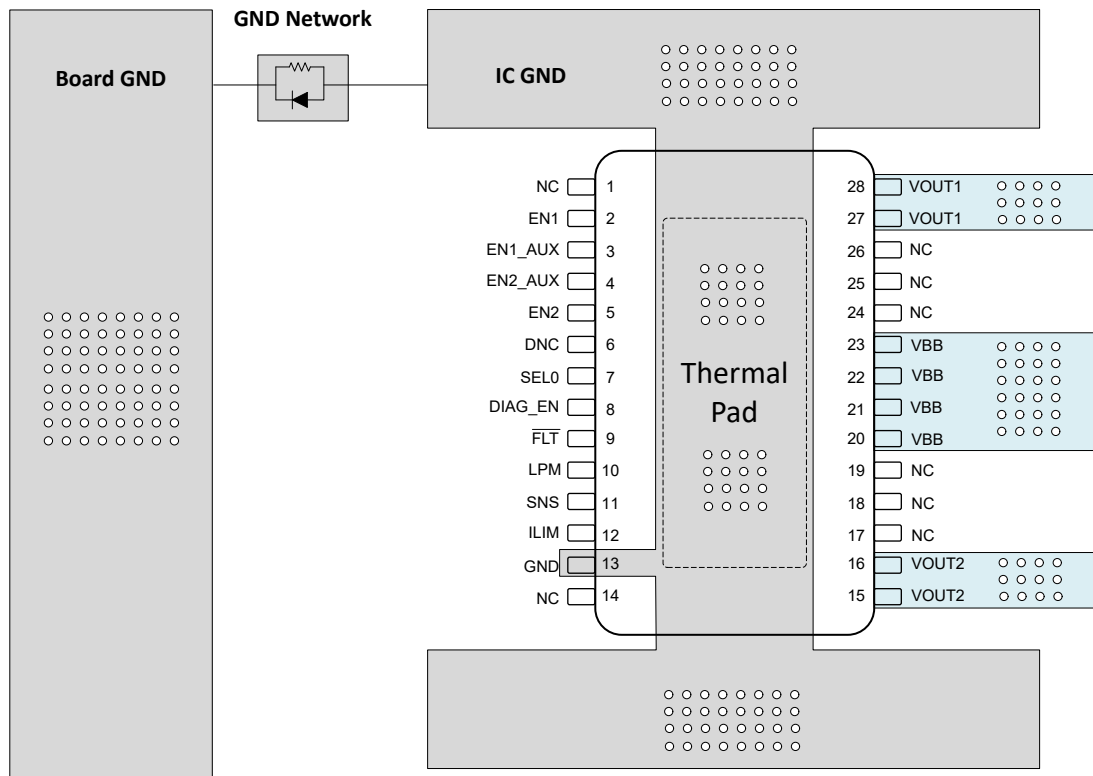


Figure 8-6. Layout Example With a GND Network

9 Device and Documentation Support

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This integrated circuit can be damaged by ESD. Texas Instruments recommends that all integrated circuits be handled with appropriate precautions. Failure to observe proper handling and installation procedures can cause damage.

ESD damage can range from subtle performance degradation to complete device failure. Precision integrated circuits may be more susceptible to damage because very small parametric changes could cause the device not to meet its published specifications.

9.6 Glossary

[TI Glossary](#) This glossary lists and explains terms, acronyms, and definitions.

10 Revision History

NOTE: Page numbers for previous revisions may differ from page numbers in the current version.

Changes from Revision A (August 2025) to Revision B (October 2026)	Page
• Updated the title to include 2A and automotive feature.....	1
• Updated the numbering format for tables, figures, and cross-references throughout the document.....	1
• Changed maximum selectable current limit from 5A to 4.7A.....	1
• Added functional safety capable information.....	1
• Changed output load current when both channels are enabled from up to 2.5A to up to 2A.....	1
• Changed selectable current limit settings maximum from 5A to 4.7A.....	1
• Changed low R_{ON} from 120mΩ to 130mΩ.....	1
• Changed part number from TPS2HC120A to TPS2HC120A-Q1.....	3
• Changed part number from TPS2HC120B to TPS2HC120B-Q1.....	3
• Changed pin number 7 name from SEL to SEL0.....	4
• Deleted $\overline{FAULT}$ from pin 9 $\overline{FLT}$	4
• Updated description for Thermal Pad.....	4
• Added inductive energy plots to typical characteristics.....	12
• Added Figure 7-2	17
• Updated accurate current sense.....	22

• Changed column one header from Allowed Resistor Value to Allowed Range of Resistor Values.....	24
• Changed ILIM thresholds to correspond with new allowed range of resistor values.....	24
• Changed allow range of resistor values open from > 60kΩ to > 87kΩ.....	24
• Updated inductive-load switching-off clamp.....	26
• Updated channel off.....	30
• Deleted latch version from thermal protection behavior and Figure 7-19	32
• Updated loss of device GND.....	34
• Updated loss of module GND.....	34
• Added IC to case 1.....	34
• Changed from I _{C_GND} to IC GND.....	34
• Updated Loss of Battery.....	36
• Updated SLEEP.....	39
• Deleted FLT pin information from ACTIVE.....	40
• Moved EMC Transient Disturbances Test from after Application Curves to after Application Information.....	41
• Changes C _{IC} description from 100nF to 15nF.....	41
• Added Figure 8-3	43

Changes from Revision * (March 2025) to Revision A (August 2025)	Page
• Changed TPS2HC120B from preview to production data.....	3

11 Mechanical, Packaging, and Orderable Information

The following pages include mechanical, packaging, and orderable information. This information is the most-current data available for the designated device. This data is subject to change without notice and without revision of this document. For browser-based versions of this data sheet, see the left-hand navigation pane.

PACKAGING INFORMATION

Orderable part number	Status (1)	Material type (2)	Package Pins	Package qty Carrier	RoHS (3)	Lead finish/ Ball material (4)	MSL rating/ Peak reflow (5)	Op temp (°C)	Part marking (6)
TPS2HC120AQDGQRQ1	Active	Production	HVSSOP (DGQ) 28	2500 LARGE T&R	Yes	NIPDAU	Level-3-260C-168 HR	-40 to 125	2HC120A
TPS2HC120AQDGQRQ1.A	Active	Production	HVSSOP (DGQ) 28	2500 LARGE T&R	Yes	NIPDAU	Level-3-260C-168 HR	-40 to 125	2HC120A
TPS2HC120BQDGQRQ1	Active	Production	HVSSOP (DGQ) 28	2500 LARGE T&R	Yes	NIPDAU	Level-3-260C-168 HR	-40 to 125	2HC120B

⁽¹⁾ **Status:** For more details on status, see our [product life cycle](#).

⁽²⁾ **Material type:** When designated, preproduction parts are prototypes/experimental devices, and are not yet approved or released for full production. Testing and final process, including without limitation quality assurance, reliability performance testing, and/or process qualification, may not yet be complete, and this item is subject to further changes or possible discontinuation. If available for ordering, purchases will be subject to an additional waiver at checkout, and are intended for early internal evaluation purposes only. These items are sold without warranties of any kind.

⁽³⁾ **RoHS values:** Yes, No, RoHS Exempt. See the [TI RoHS Statement](#) for additional information and value definition.

⁽⁴⁾ **Lead finish/Ball material:** Parts may have multiple material finish options. Finish options are separated by a vertical ruled line. Lead finish/Ball material values may wrap to two lines if the finish value exceeds the maximum column width.

⁽⁵⁾ **MSL rating/Peak reflow:** The moisture sensitivity level ratings and peak solder (reflow) temperatures. In the event that a part has multiple moisture sensitivity ratings, only the lowest level per JEDEC standards is shown. Refer to the shipping label for the actual reflow temperature that will be used to mount the part to the printed circuit board.

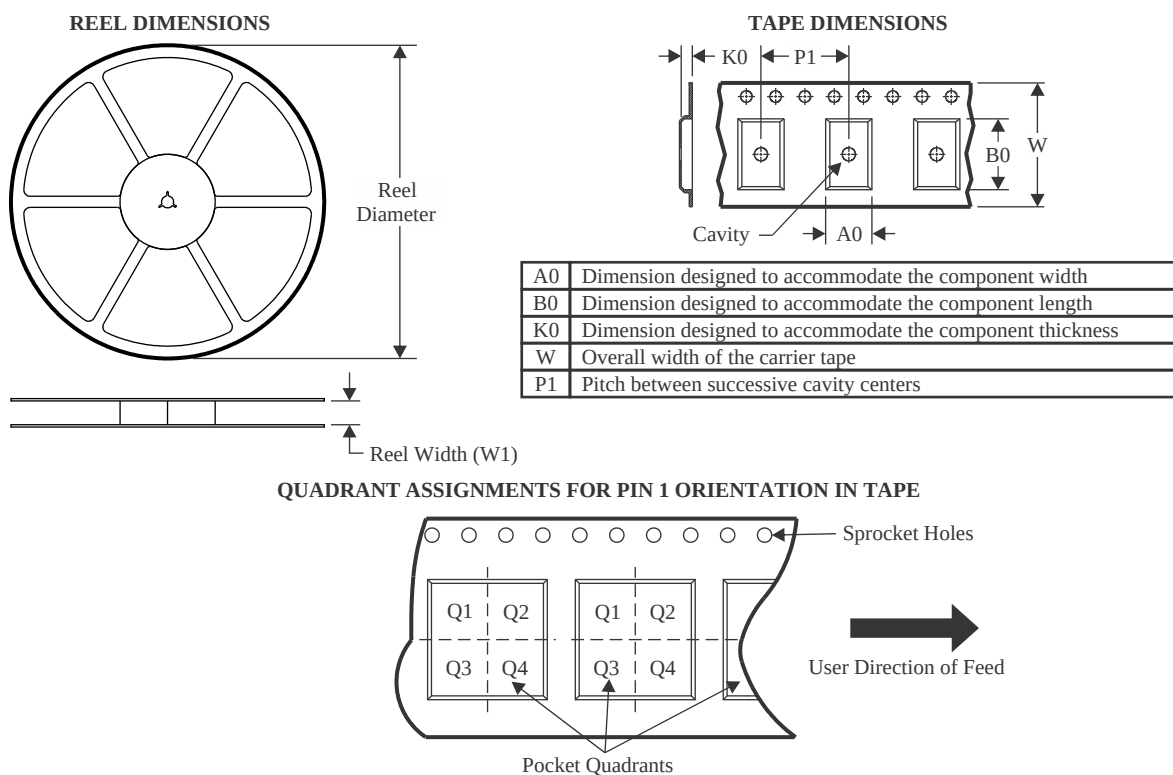
⁽⁶⁾ **Part marking:** There may be an additional marking, which relates to the logo, the lot trace code information, or the environmental category of the part.

Multiple part markings will be inside parentheses. Only one part marking contained in parentheses and separated by a "~" will appear on a part. If a line is indented then it is a continuation of the previous line and the two combined represent the entire part marking for that device.

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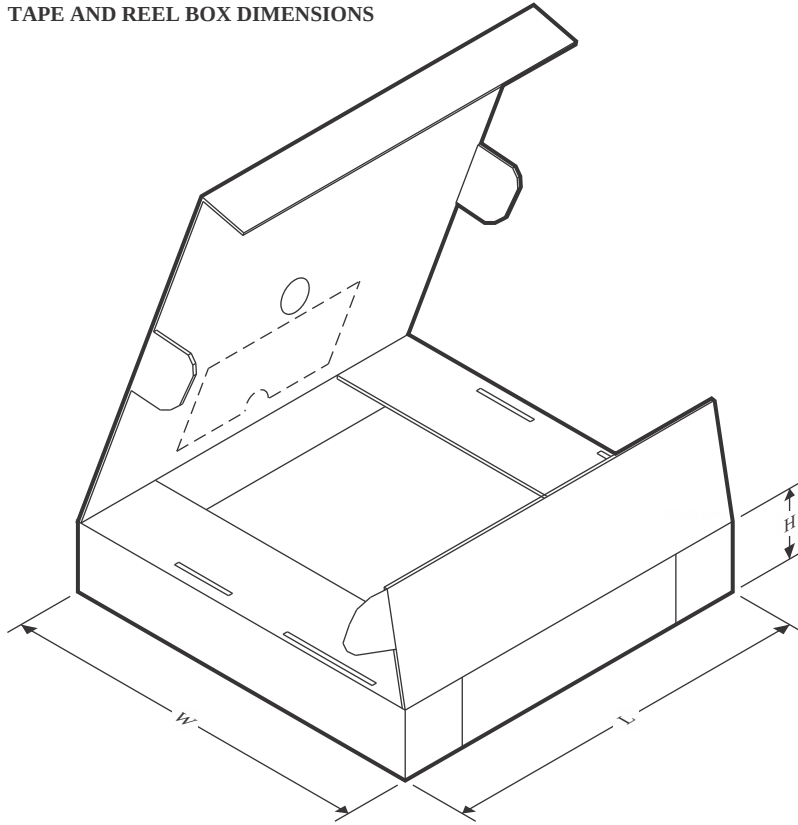
TAPE AND REEL INFORMATION



*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Reel Diameter (mm)	Reel Width W1 (mm)	A0 (mm)	B0 (mm)	K0 (mm)	P1 (mm)	W (mm)	Pin1 Quadrant
TPS2HC120AQDGQRQ1	HVSSOP	DGQ	28	2500	330.0	16.4	5.5	7.4	1.45	8.0	16.0	Q1
TPS2HC120BQDGQRQ1	HVSSOP	DGQ	28	2500	330.0	16.4	5.5	7.4	1.45	8.0	16.0	Q1

TAPE AND REEL BOX DIMENSIONS



*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Length (mm)	Width (mm)	Height (mm)
TPS2HC120AQDGQRQ1	HVSSOP	DGQ	28	2500	353.0	353.0	32.0
TPS2HC120BQDGQRQ1	HVSSOP	DGQ	28	2500	353.0	353.0	32.0

GENERIC PACKAGE VIEW

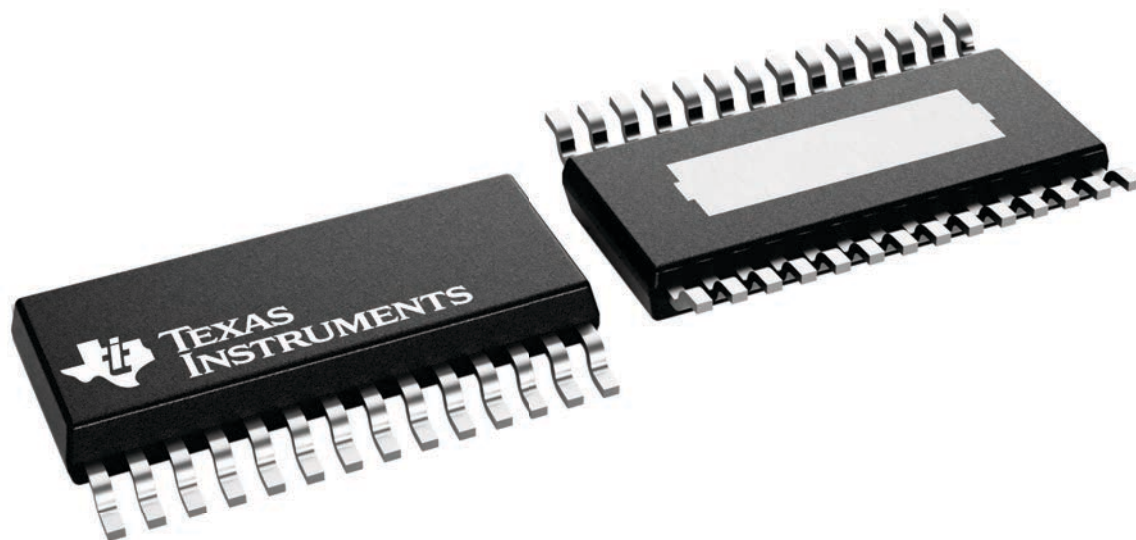
DGQ 28

HVSSOP - 1.1 mm max height

3 x 7.1, 0.5 mm pitch

SMALL OUTLINE PACKAGE

This image is a representation of the package family, actual package may vary.
Refer to the product data sheet for package details.



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