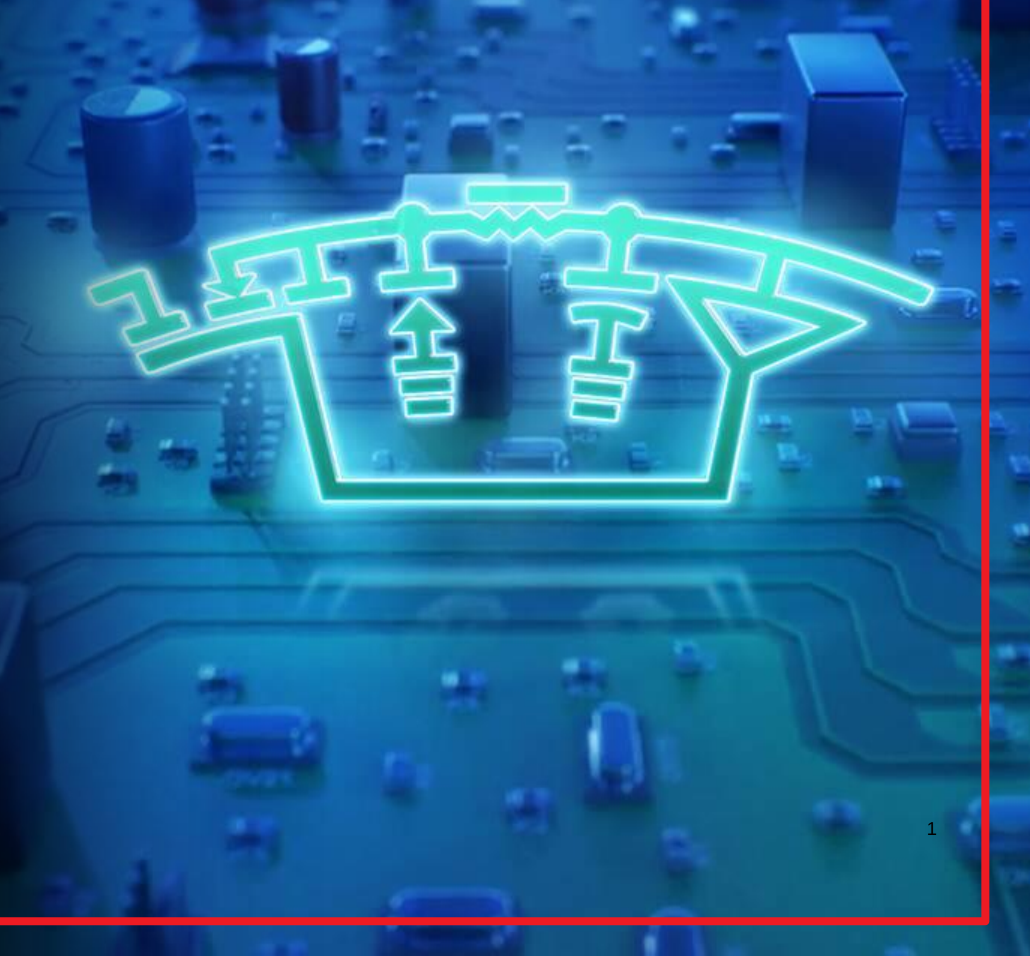
Power Supply Design Seminar

Switch-mode power converter compensation made easy



Authors

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Agenda

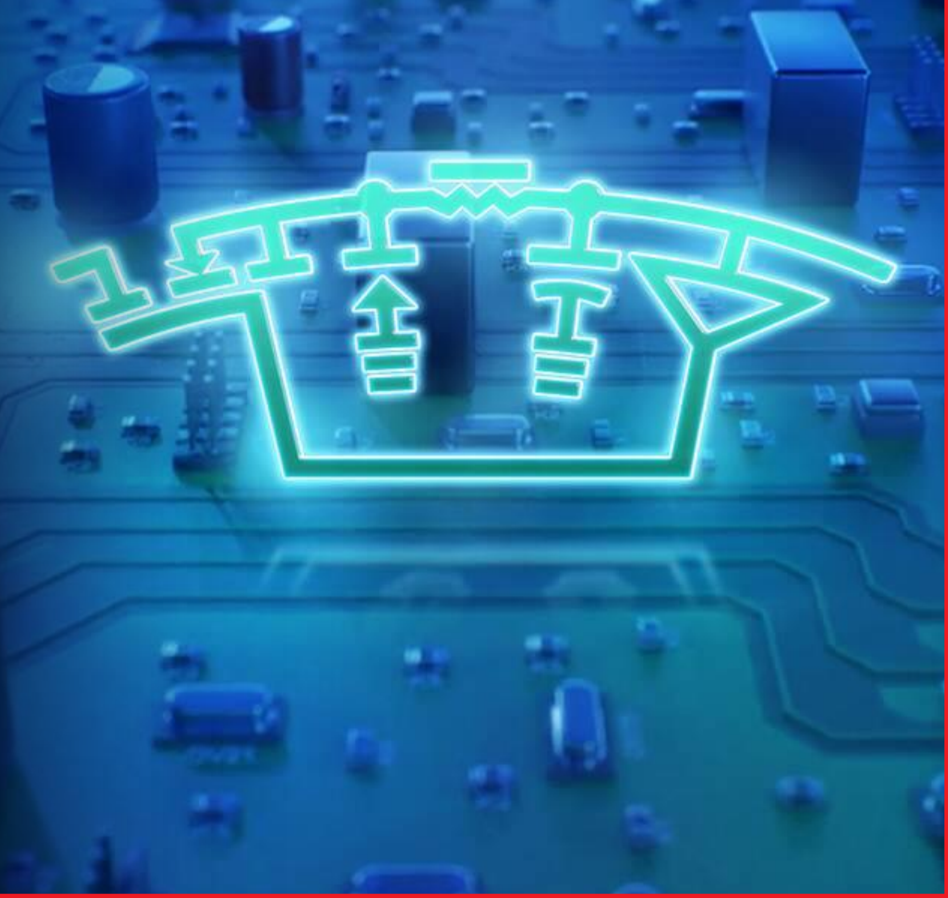
Texas Instruments

Introduction

Feature presentation

Live Q&A session

Enter questions into chat at any time



2025 Power Supply Design Seminar

Texas Instruments

Webinar Series

April 30	Common mistakes in DC/DC converters and how to fix them
May 28	Survey of resonant converter topologies
June 25	**Power Factor Correction (PFC) circuit basics**
July 30	Power-conversion techniques for complying with automotive emissions requirements
August 27	Switch-mode power converter compensation made easy
September 24	Constructing your power supply – layout considerations

Last Wednesday of every month
8:00AM & 8:00PM (US Central Time Zone)

Welcome to the PSDS 2025 webinar series!

TEXAS INSTRUMENTS

The history of Power Supply Design Seminar

- In 1977 Bob Mammano, the “Father of PWM Industry,” started the seminar
- 47+ years
- 26+ seminars
- 100+ technical topics
- 50,000+ customers
- A comprehensive archive of white papers, presentations and videos

Power supply industry legends associated with PSDS:
Bob Mammano, Lloyd Dixon, Bill Andreycak, Robert Kollman, Laszlo Balogh

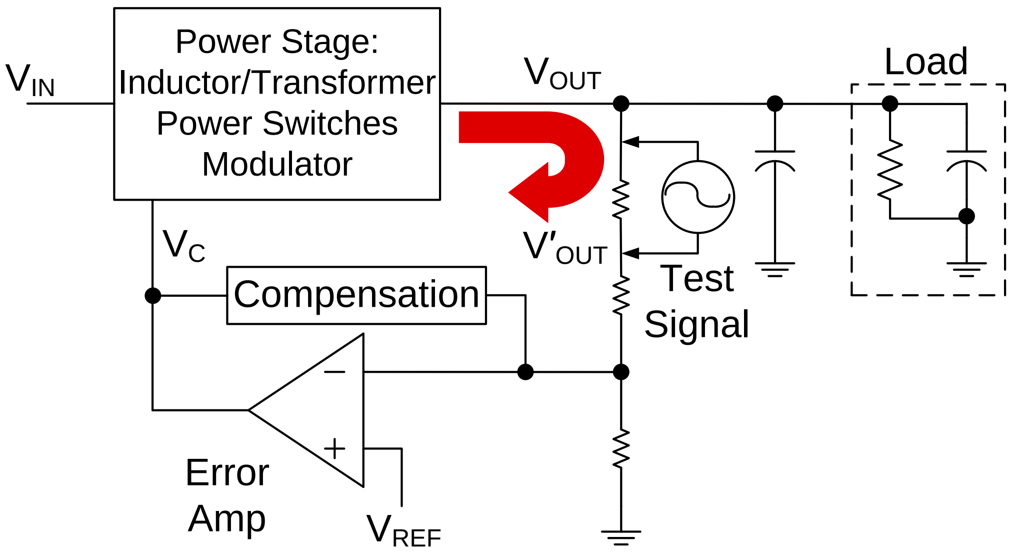
WWW.TI.COM/PSDS for all prior content

Agenda

- Compensation design and objective
- Explanation of poles and zeros
- Power stage characteristics
- Error amplifier and transconductance amplifier
- Isolated feedback with opto-coupler
- Compensation examples
- Circuit limitations and other issues

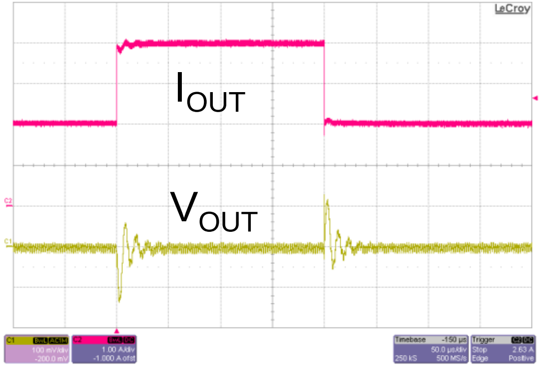
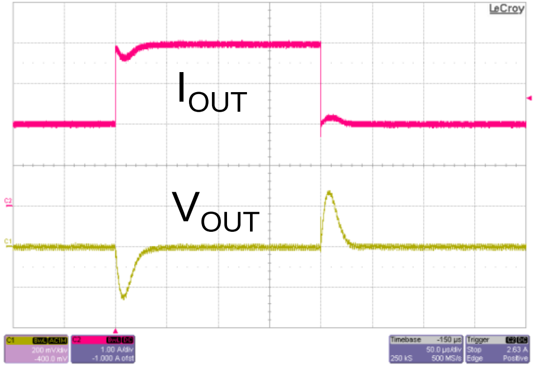
Compensation design and objectives

Why do we need feedback and why do we need compensation?

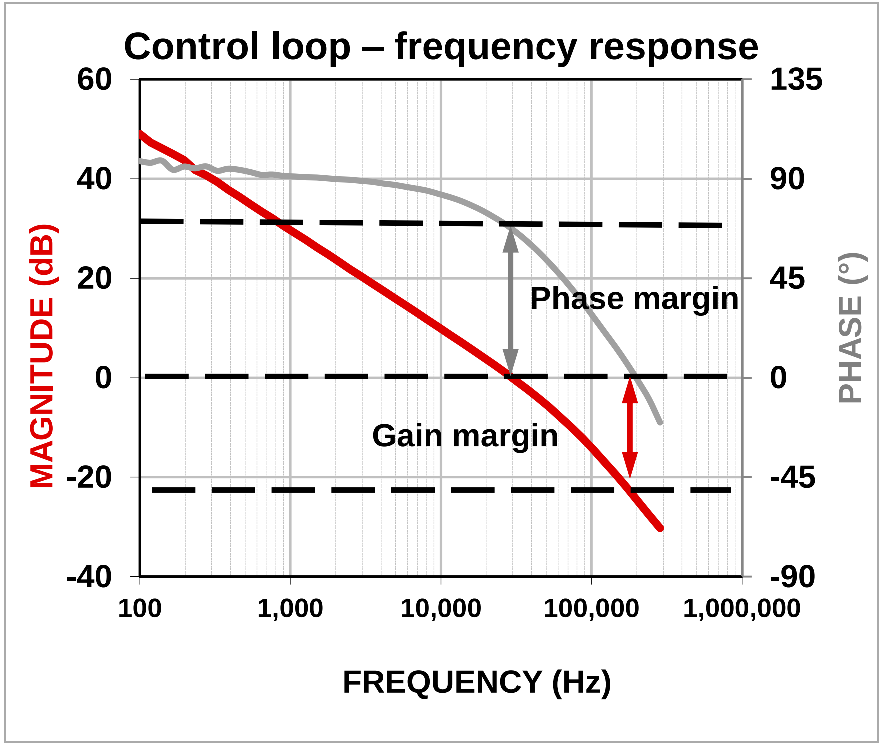


- Feedback is needed to regulate the output voltage
- The control loop bandwidth influences the response time

Control loop response

Poor transient response	Objective	Good transient response
 • Response is under-damped causing oscillatory behavior	• Maximize crossover frequency for fastest transient response • Adjust compensation for best setting behavior	 • Response is well damped with good setting behavior

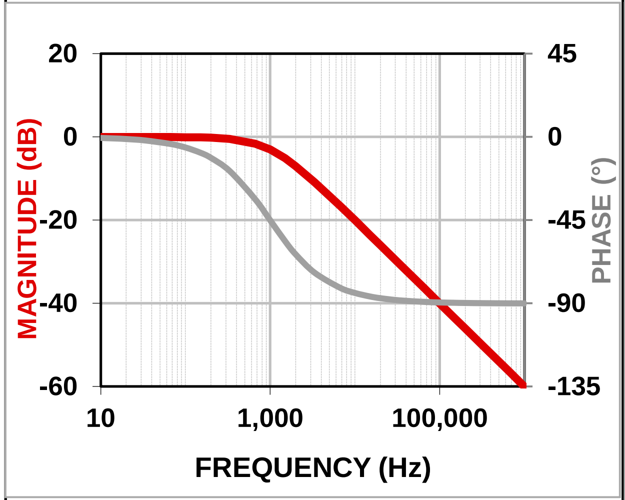
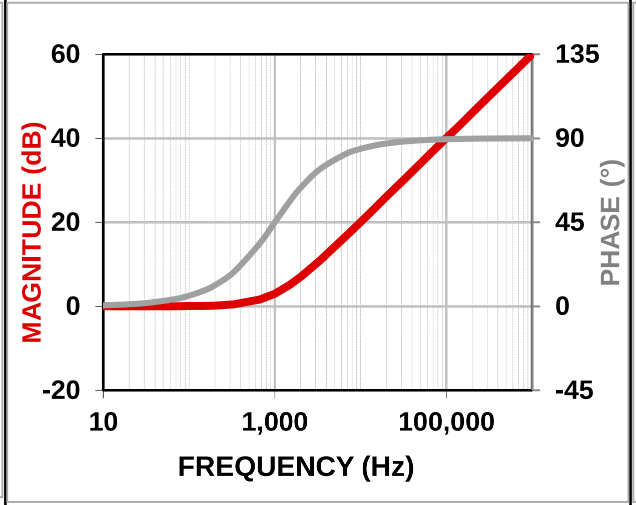
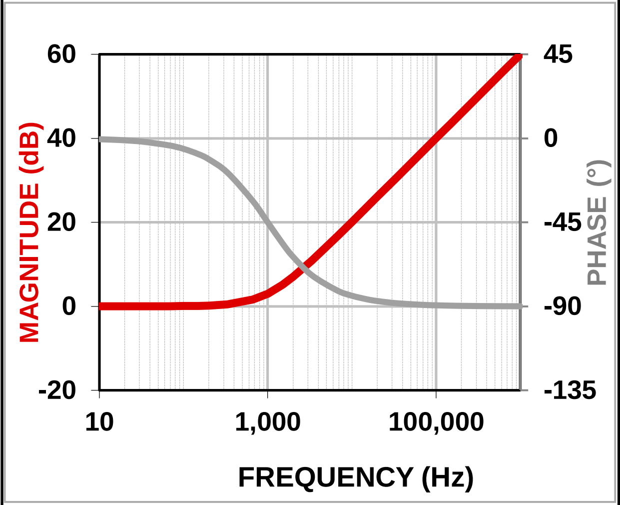
Phase margin and gain margin



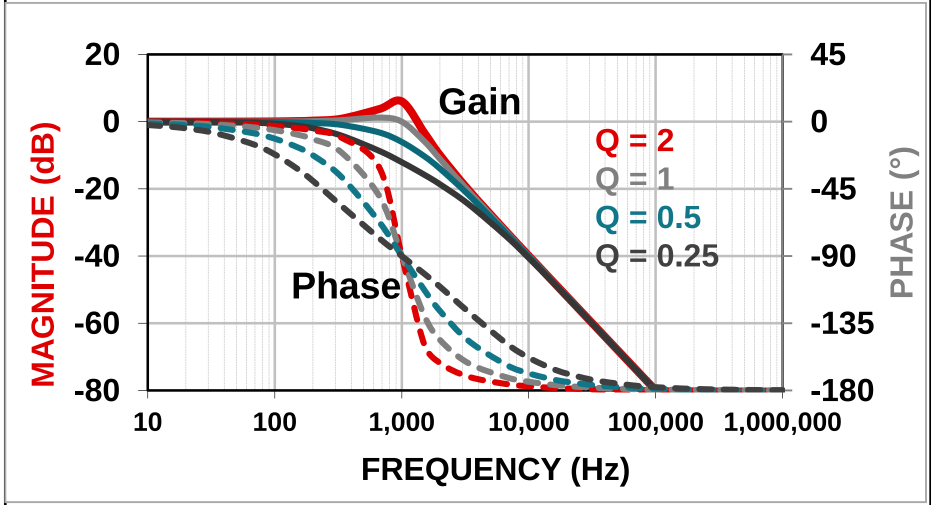
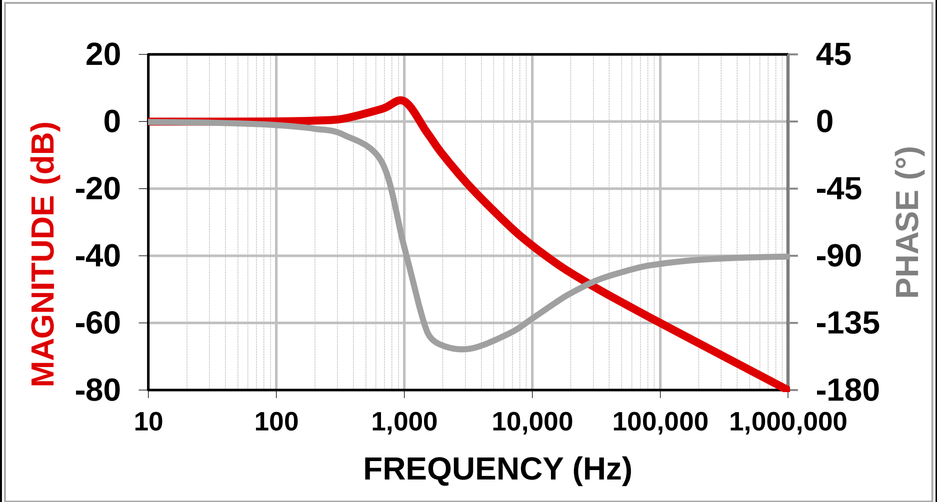
Phase margin and stability

- Sufficient phase margin needed to prevent oscillation (45° min.)
- Gain margin goal of 10 dB min.
- Slope of -20dB/decade when passing through 0 dB
- Bandwidth rule of thumb is 1/5 to 1/10 of switching frequency

Poles, zeros and right-half-plane zeros

Pole	Zero	Right-half-plane zero
$H(s) = \dfrac{1}{1 + \dfrac{s}{\omega_P}}$	$H(s) = \dfrac{1 + \dfrac{s}{\omega_Z}}{1}$	$H(s) = \dfrac{1 - \dfrac{s}{\omega_Z}}{1}$
		

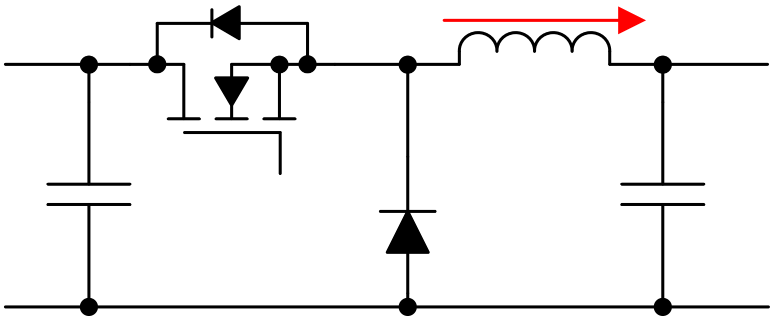
Complex conjugate pole and ESR zero

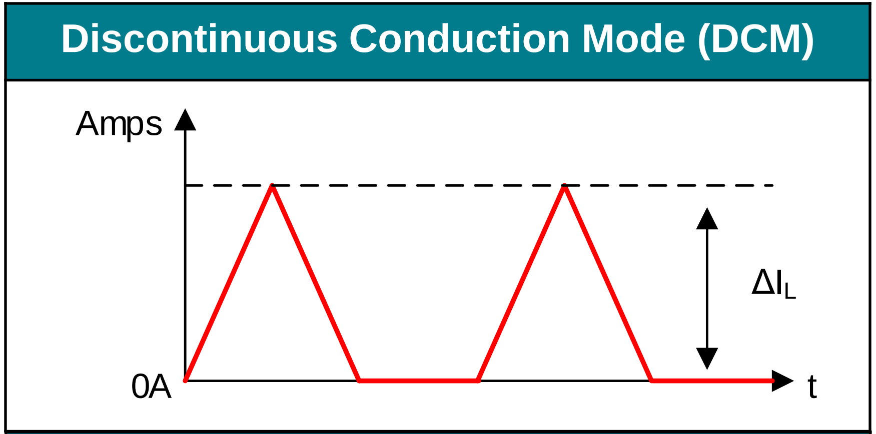
Complex conjugate pole	With ESR zero
$H(s) = \dfrac{1}{1 + \dfrac{s}{Q_0 \cdot \omega_0} + \dfrac{s^2}{\omega_0^2}}$	$H(s) = \dfrac{1 + \dfrac{s}{\omega_Z}}{1 + \dfrac{s}{Q_0 \cdot \omega_0} + \dfrac{s^2}{\omega_0^2}}$
	

Control methods and operating modes

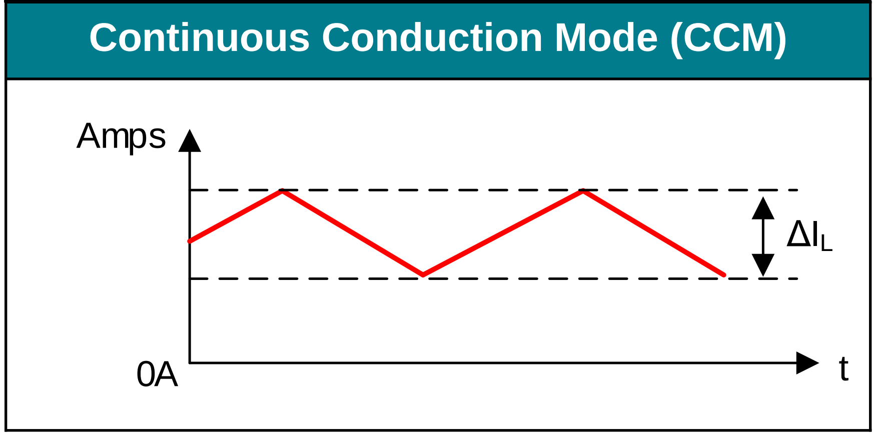
Control methods	• Voltage-mode control • Current-mode control
Operating modes	• Fixed frequency • Continuous conduction-mode (CCM)
Switching frequency and period	• Switching frequency – f_{SW} • Switching period – T $T = \frac{1}{f_{sw}}$

DCM vs CCM





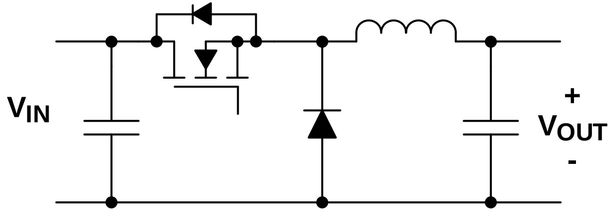
Discontinuous Conduction Mode (DCM)
Amps
ΔIL
0A
t



Continuous Conduction Mode (CCM)
Amps
ΔIL
0A
t

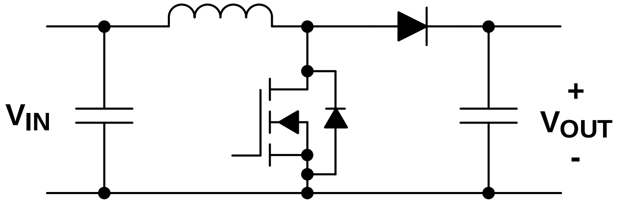
Buck, boost, and buck-boost derived topologies

Buck, forward, push-pull, bridge



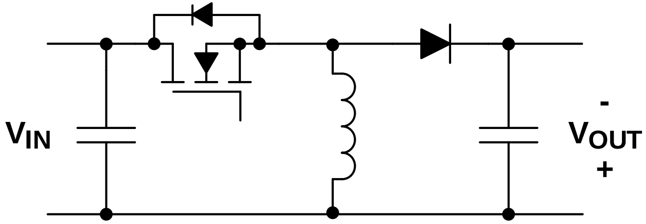
$$V_{OUT} = V_{IN} \times D$$

Boost



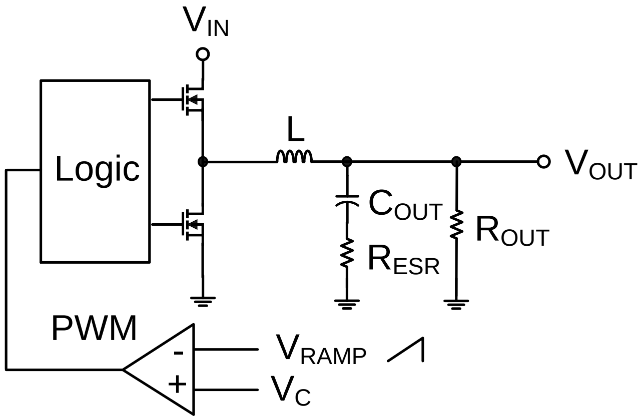
$$V_{OUT} = V_{IN} \times \frac{1}{1-D}$$

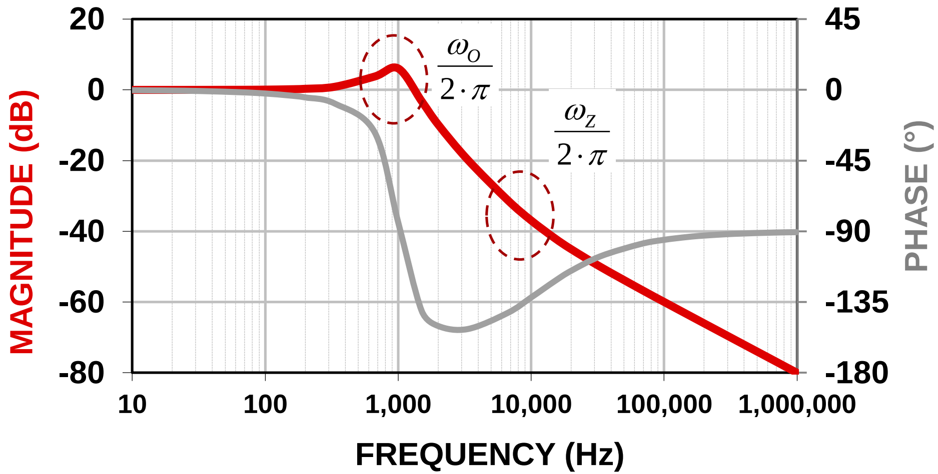
Buck-boost, SEPIC, flyback



$$V_{OUT} = V_{IN} \times \frac{D}{1-D}$$

Voltage-mode buck power stage





$$A_{VC} = \frac{V_{IN}}{V_{RAMP}}$$

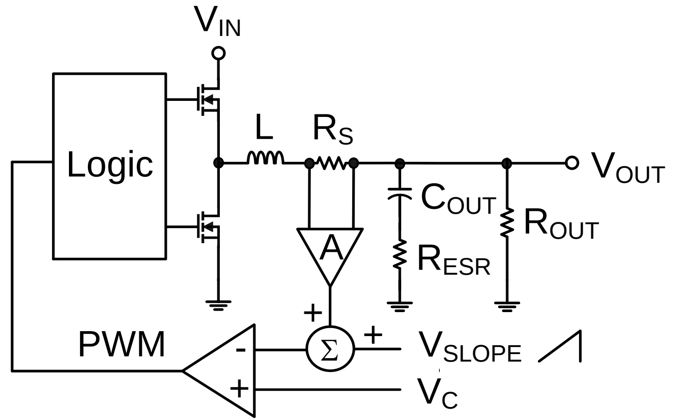
$$\omega_O = \frac{1}{\sqrt{L \cdot C_{OUT}}}$$

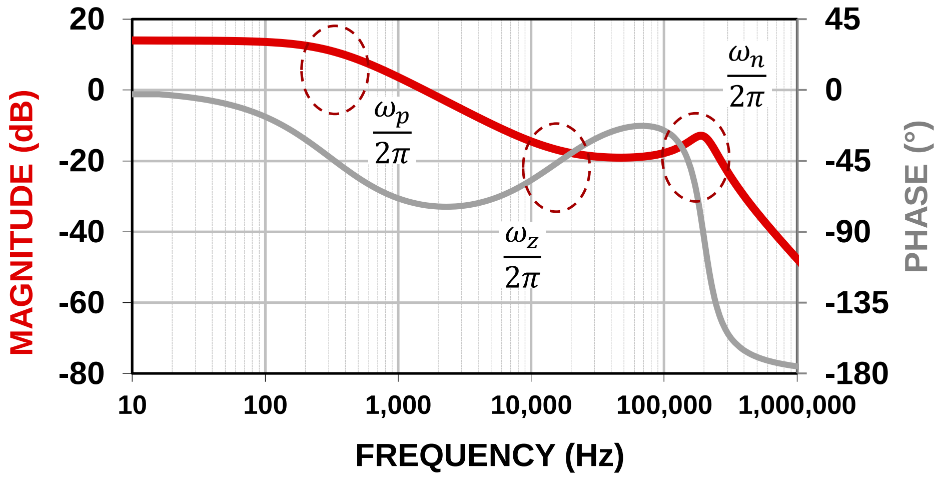
$$Q_O = \frac{R_{OUT}}{\sqrt{L / C_{OUT}}}$$

$$\omega_Z = \frac{1}{R_{ESR} \cdot C_{OUT}}$$

$$\frac{\hat{v}_{OUT}}{\hat{v}_C} = A_{VC} \cdot \frac{1 + \frac{s}{\omega_Z}}{1 + \frac{s}{Q_O \cdot \omega_O} + \frac{s^2}{\omega_O^{\,2}}}$$

Current-mode buck power stage





$$\omega_p \approx \frac{1}{C_{out} \cdot R_{out}}$$

$$\omega_z = \frac{1}{R_{ESR} \cdot C_{out}}$$

$$A_{VC} \approx \frac{R_{out}}{R_i} = \frac{R_{out}}{A \cdot R_S}$$

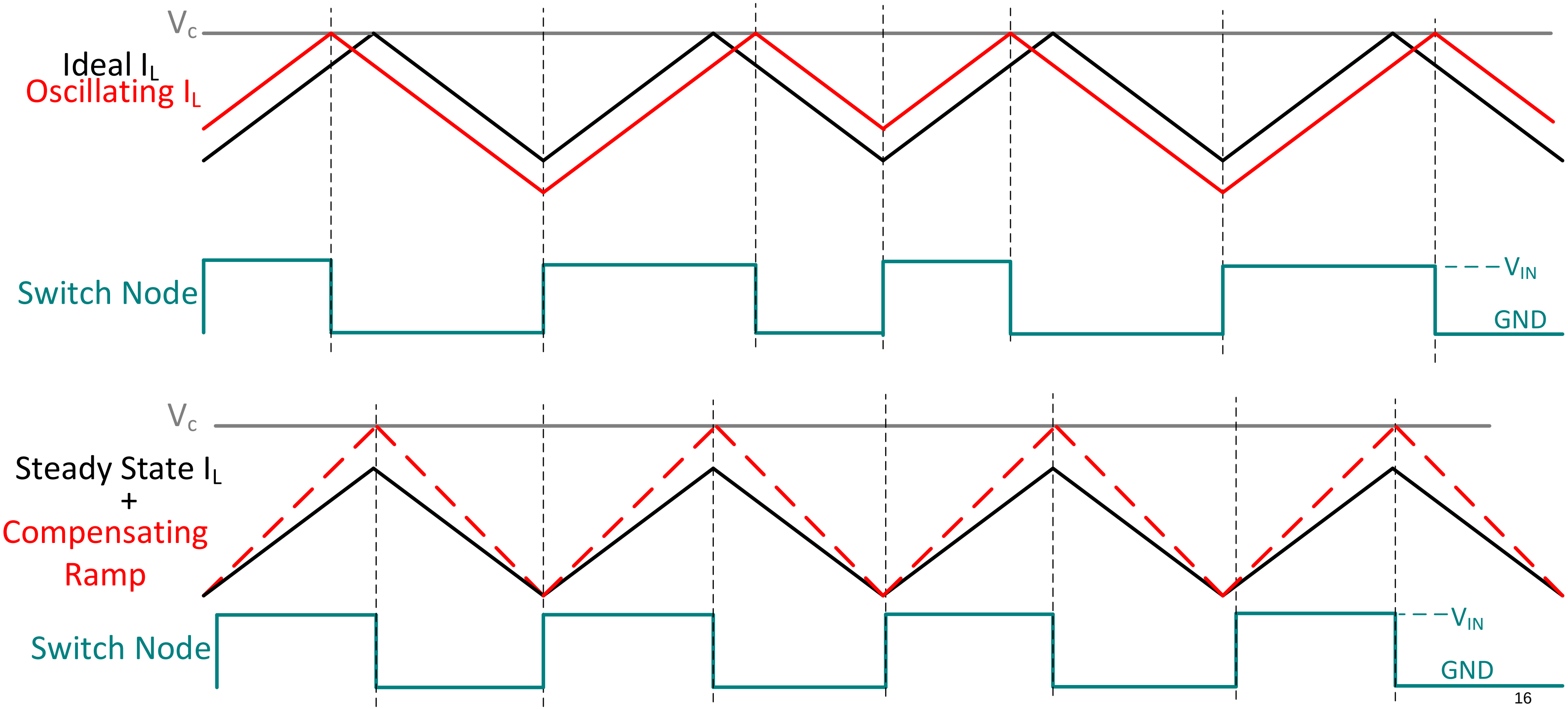
$$F_h(s) = \frac{1}{1 + \frac{s}{\omega_n \cdot Q_p} + \left(\frac{s}{\omega_n}\right)^2}$$

$$\omega_n = \frac{\omega_{fsw}}{2}$$

at D = 0.5

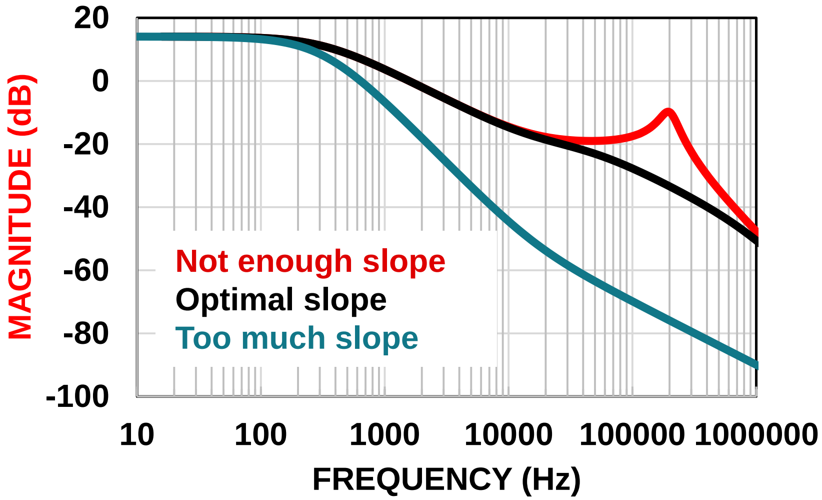
$$\frac{\hat{v}_{out}}{\hat{v}_c} \approx A_{VC} \cdot \frac{1 + \frac{s}{\omega_z}}{1 + \frac{s}{\omega_p}} \cdot F_h(s)$$

Why is slope compensation needed?

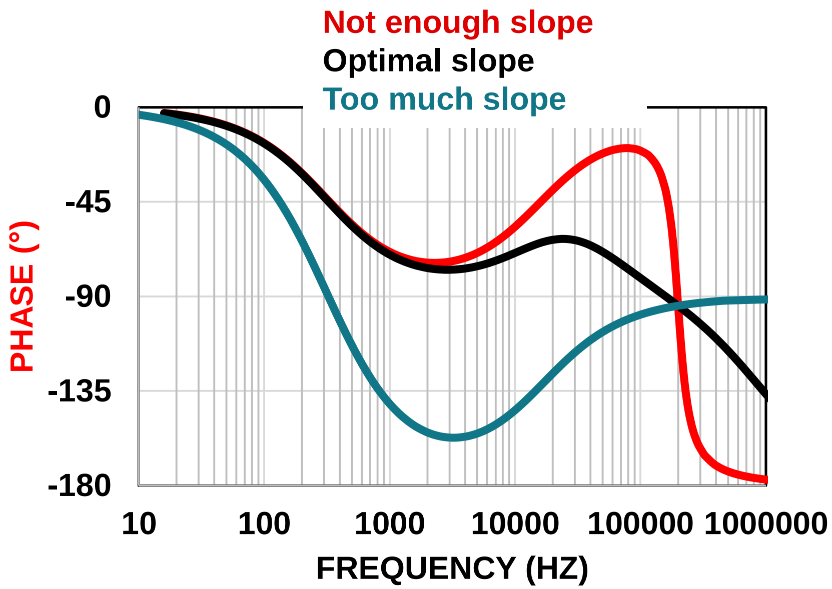


Impact of Slope Compensation

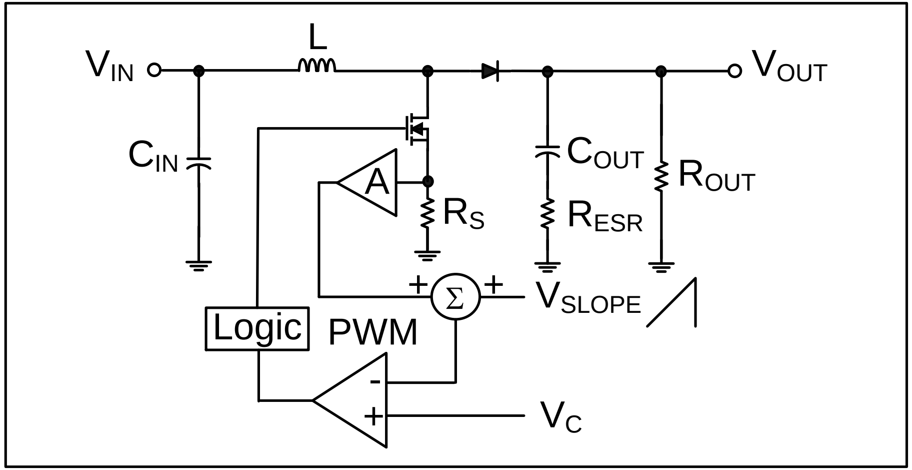
Gain	Phase

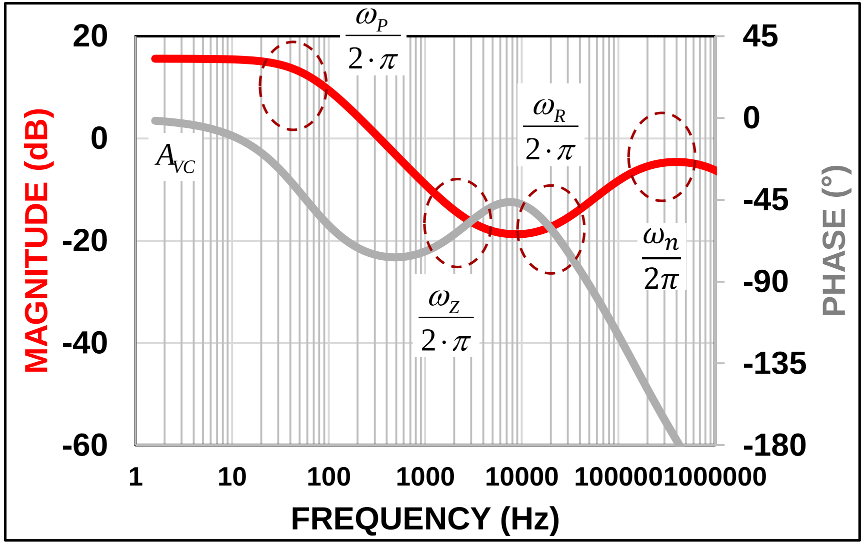


*gain curves normalized to 14 dB DC gain



Current-mode boost power stage





$$R_i = A \cdot R_S$$

$$\omega_r \approx \frac{R_{out}\cdot(1-D)^2}{L}$$

$$\omega_n = \frac{\omega_{fsw}}{2}$$

$$A_{VC} \approx \frac{R_{out}\cdot(1-D)}{R_i}$$

$$\omega_Z = \frac{1}{R_{ESR}\cdot C_{OUT}}$$

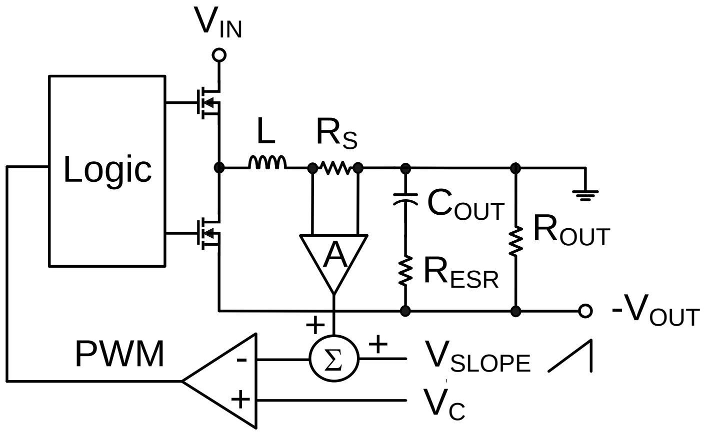
at D = 0.5

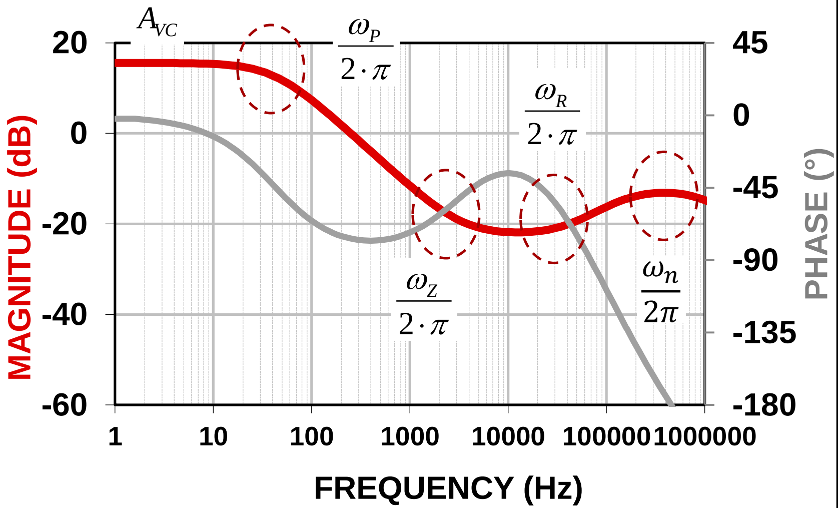
$$\omega_P \approx \frac{2}{C_{OUT}\cdot R_{OUT}}$$

$$F_h(s) = \frac{1}{1+\frac{s}{\omega_n\cdot Q_p}+\left(\frac{s}{\omega_n}\right)^2}$$

$$\frac{\hat{v}_{out}}{\hat{v}_c} \approx A_{VC}\cdot\frac{\left(1+\frac{s}{\omega_z}\right)\left(1-\frac{s}{\omega_r}\right)}{1+\frac{s}{\omega_p}}\cdot F_h(s)$$

Current-mode buck-boost power stage





$$R_i = A \cdot R_S$$

$$\omega_r \approx \frac{R_{out}\cdot(1-D)^2}{L\cdot D}$$

$$A_{VC} \approx \frac{R_{out}\cdot(1-D)}{(1-D)\cdot R_i}$$

$$\omega_Z = \frac{1}{R_{ESR}\cdot C_{OUT}}$$

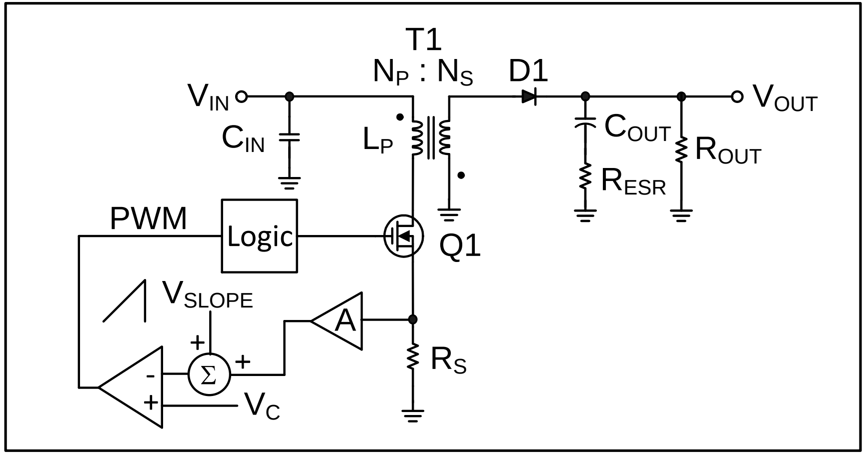
at D = 0.5

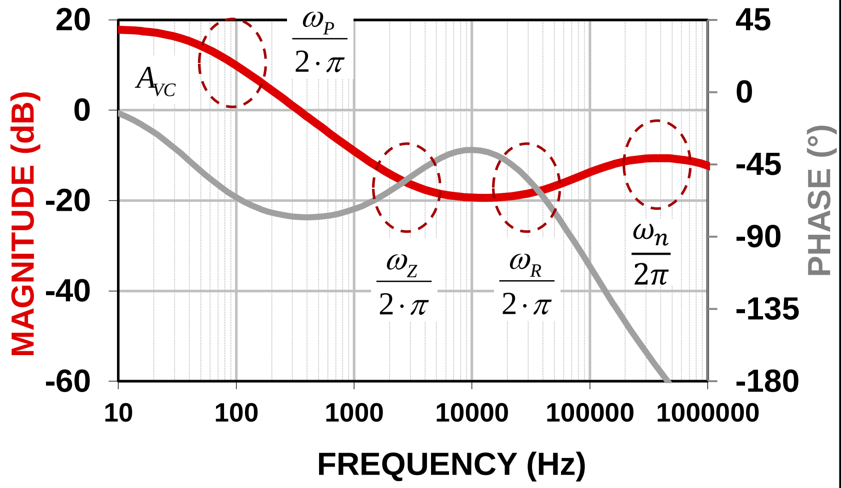
$$\omega_P \approx \frac{1+D}{C_{OUT}\cdot R_{OUT}}$$

$$F_h(s) = \frac{1}{1+\frac{s}{\omega_n\cdot Q_p}+\left(\frac{s}{\omega_n}\right)^2}$$

$$\frac{\hat{v}_{out}}{\hat{v}_c} \approx A_{VC}\cdot\frac{\left(1+\frac{s}{\omega_z}\right)\left(1-\frac{s}{\omega_r}\right)}{1+\frac{s}{\omega_p}}\cdot F_h(s)$$

Current-mode flyback power stage





$$R_i = A \cdot R_S$$

$$\omega_r \approx \frac{R_{out} \cdot (1-D)^2}{L \cdot D}$$

$$A_{VC} \approx \frac{R_{out} \cdot (1-D)}{(1-D) \cdot R_i} \cdot \frac{N_P}{N_S}$$

$$\omega_Z = \frac{1}{R_{ESR} \cdot C_{OUT}}$$

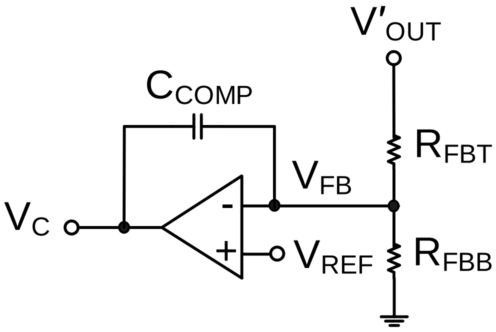
at D = 0.5

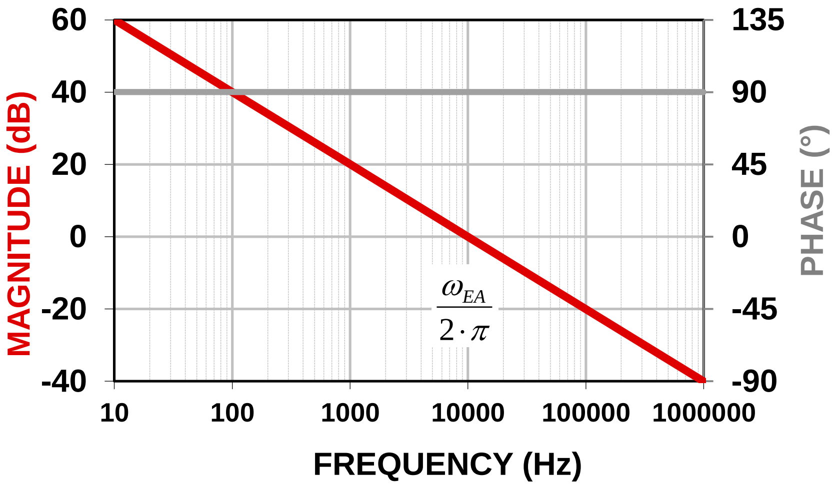
$$\omega_P \approx \frac{1+D}{C_{OUT} \cdot R_{OUT}}$$

$$F_h(s) = \frac{1}{1 + \frac{s}{\omega_n \cdot Q_p} + \left(\frac{s}{\omega_n}\right)^2}$$

$$\frac{\hat{v}_{out}}{\hat{v}_c} \approx A_{VC} \cdot \frac{\left(1 + \frac{s}{\omega_Z}\right)\left(1 - \frac{s}{\omega_r}\right)}{1 + \frac{s}{\omega_p}} \cdot F_h(s)$$

Type I error amplifier

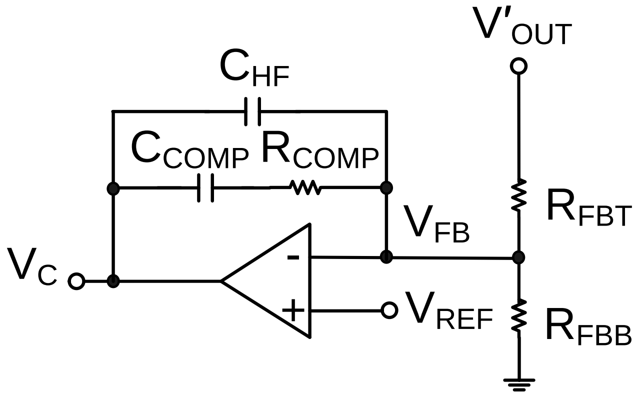


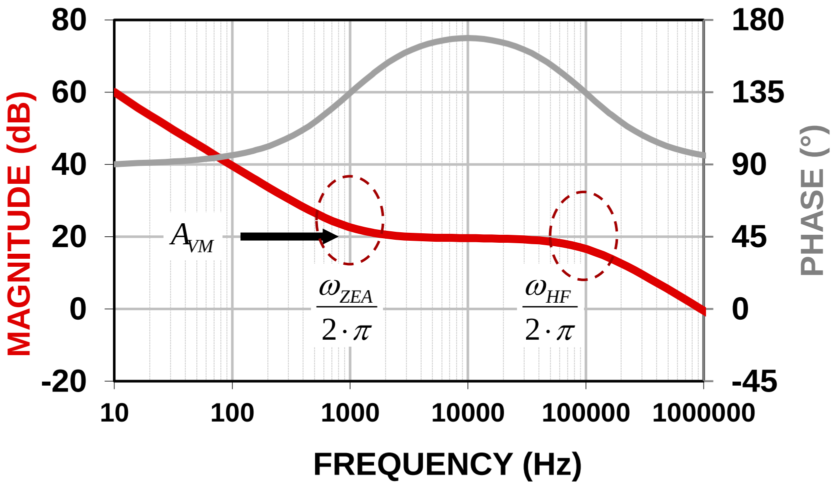


$$\omega_{EA} = \frac{1}{R_{FBT} \cdot C_{COMP}}$$

$$\frac{\hat{v}_C}{\hat{v}'_{OUT}} \approx -\frac{\omega_{EA}}{s}$$

Type II error amplifier





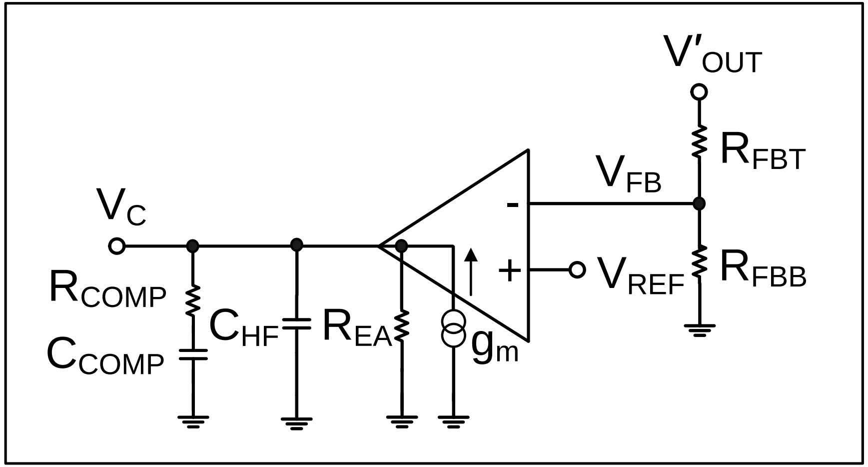
$$A_{VM} \approx \frac{R_{COMP}}{R_{FBT}} \qquad \omega_{HF} \approx \frac{1}{R_{COMP} \cdot C_{HF}}$$

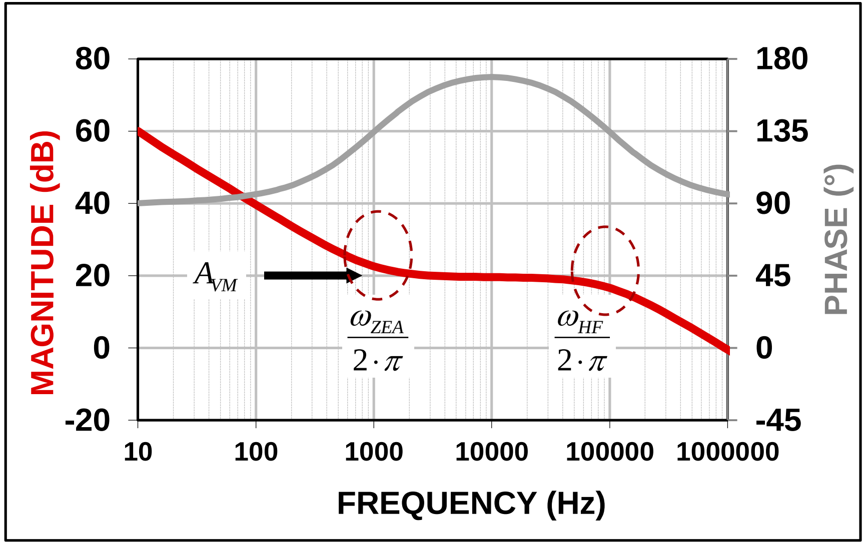
$$\omega_{ZEA} = \frac{1}{R_{COMP} \cdot C_{COMP}}$$

Assumption: $C_{COMP} >> C_{HF}$

$$\frac{\hat{v}_c}{\hat{v}'_{out}} \approx -\frac{A_{VM} \cdot \omega_{ZEA}}{s} \cdot \frac{1 + \frac{s}{\omega_{ZEA}}}{1 + \frac{s}{\omega_{HF}}}$$

Type II transconductance amplifier





$$A_{VM} = K_{FB} \cdot g_m \cdot R_{COMP}$$

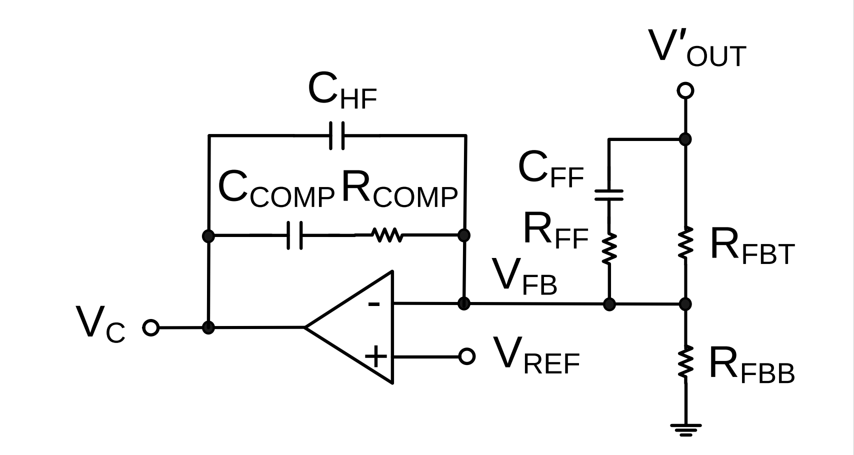
$$\omega_{ZEA} = \frac{1}{R_{COMP} \cdot C_{COMP}} \qquad K_{FB} = \frac{R_{FBB}}{R_{FBB} + R_{FBT}}$$

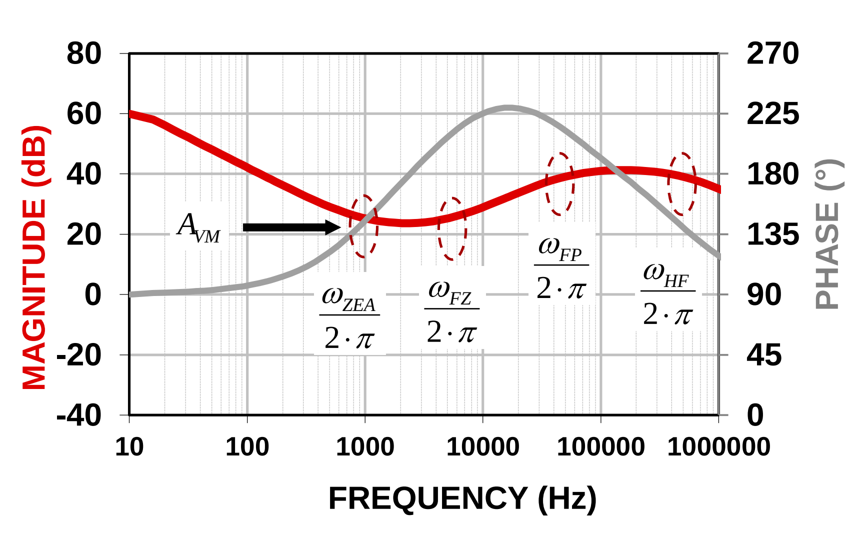
$$\omega_{HF} \approx \frac{1}{R_{COMP} \cdot C_{HF}} \qquad A_{OL} = g_m \cdot R_{EA}$$

Assumptions: $C_{COMP} >> C_{HF}$ & $R_{EA} >> R_{COMP}$

$$\frac{\hat{v}_c}{\hat{v}'_{out}} \approx -\frac{A_{VM} \cdot \omega_{ZEA}}{s} \cdot \frac{1 + \frac{s}{\omega_{ZEA}}}{1 + \frac{s}{\omega_{HF}}}$$

Type III error amplifier





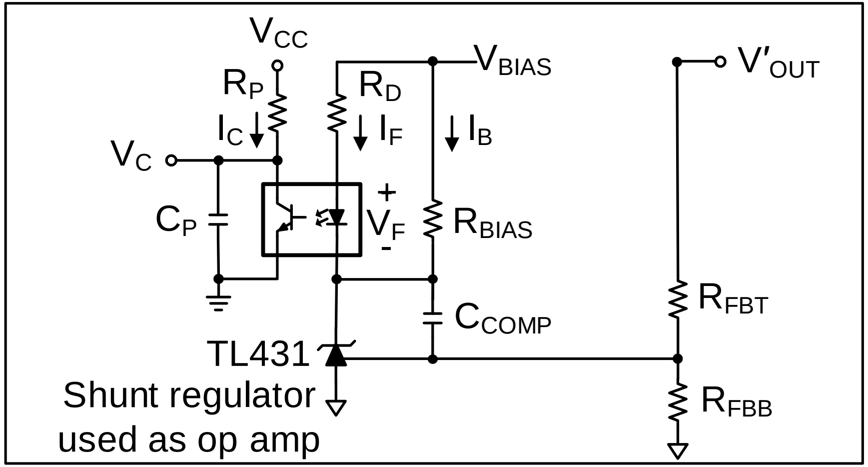
$$A_{VM} \approx \frac{R_{COMP}}{R_{FBT}} \qquad \omega_{ZEA} = \frac{1}{R_{COMP} \cdot C_{COMP}} \qquad \omega_{FP} = \frac{1}{R_{FF} \cdot C_{FF}}$$

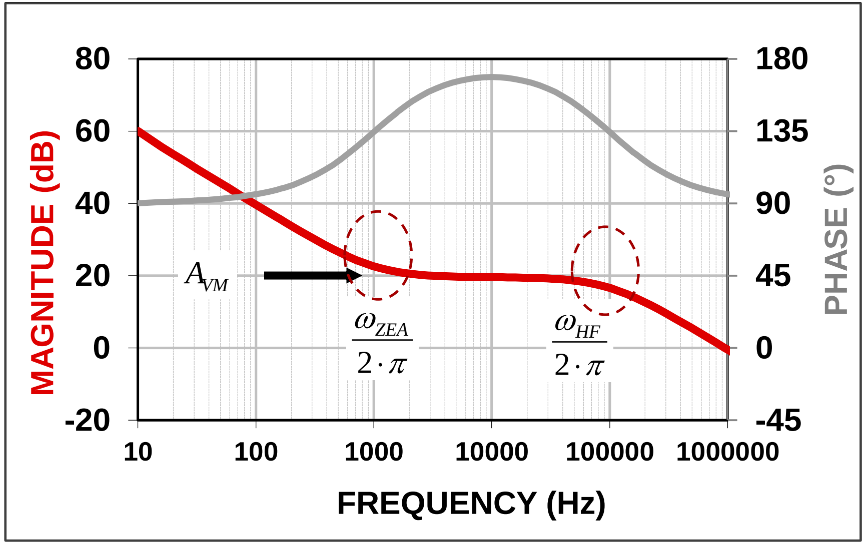
$$\omega_{FZ} \approx \frac{1}{R_{FBT} \cdot C_{FF}} \qquad \omega_{HF} \approx \frac{1}{R_{COMP} \cdot C_{HF}}$$

Assumptions: $C_{COMP} >> C_{HF}$ & $R_{FBT} >> R_{FF}$

$$\frac{\hat{v}_c}{\hat{v}'_{out}} \approx -\frac{A_{VM} \cdot \omega_{ZEA}}{s} \cdot \frac{\left(1+\frac{s}{\omega_{ZEA}}\right)\cdot\left(1+\frac{s}{\omega_{FZ}}\right)}{\left(1+\frac{s}{\omega_{FP}}\right)\cdot\left(1+\frac{s}{\omega_{HF}}\right)}$$

Type II isolated feedback with fixed bias



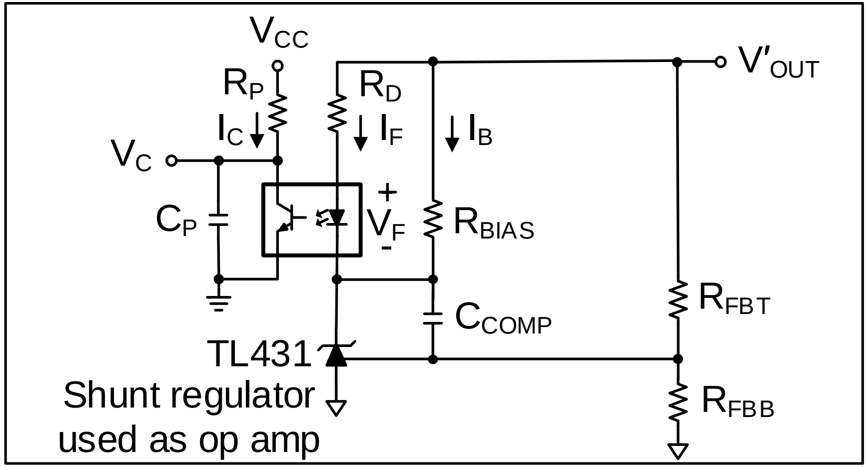


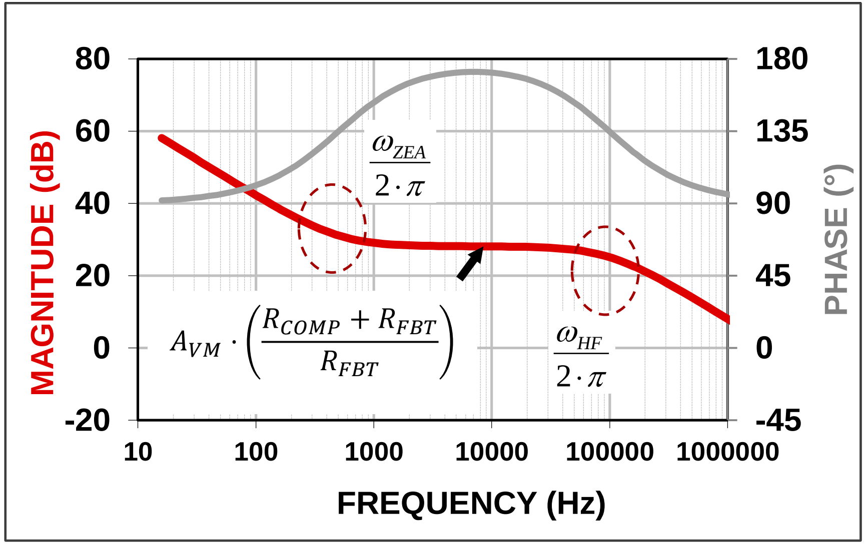
$$A_{VM} = CTR \cdot \frac{R_P}{R_D} \qquad CTR = \frac{I_C}{I_F}$$

$$\omega_{ZEA} = \frac{1}{R_{COMP} \cdot C_{COMP}} \qquad \omega_{HF} = \frac{1}{R_P \cdot C_P}$$

$$\frac{\hat{v}_C}{\hat{v}'_{OUT}} \approx \frac{A_{VM} \cdot \omega_{EA}}{s} \cdot \frac{1 + \frac{s}{\omega_{EA}}}{1 + \frac{s}{\omega_{HF}}}$$

Type II isolated feedback with Vout bias





$$A_{VM} = CTR \cdot \frac{R_P}{R_D}$$

$$CTR = \frac{I_C}{I_F}$$

$$\omega_{ZEA} = \frac{1}{(R_{COMP} + R_{FBT}) \cdot C_{COMP}}$$

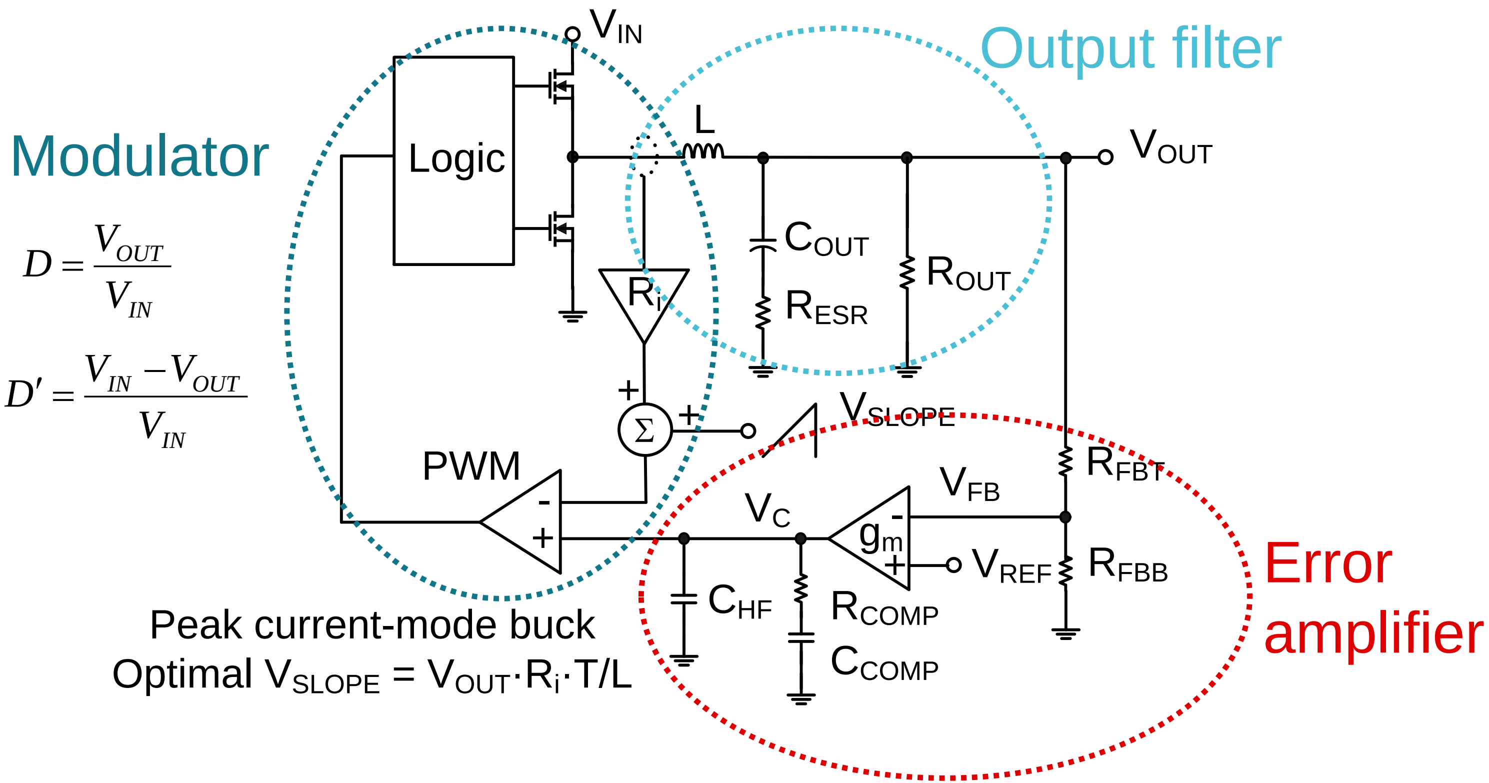
$$\omega_{HF} = \frac{1}{R_P \cdot C_P}$$

$$\frac{\hat{v}_C}{\hat{v}'_{OUT}} \approx \frac{A_{VM} \cdot \omega_{EA}}{s} \cdot \frac{1 + \frac{s}{\omega_{EA}}}{1 + \frac{s}{\omega_{HF}}}$$

Current-mode buck

$$D = \frac{V_{OUT}}{V_{IN}}$$

$$D' = \frac{V_{IN} - V_{OUT}}{V_{IN}}$$



Peak current-mode buck

Optimal $V_{SLOPE} = V_{OUT} \cdot R_i \cdot T/L$

Current-mode buck compensation strategy

- Choose a value for R_{FBT} based on bias current and power dissipation
- Find the modulator transconductance in A/V
- Pick target bandwidth, typically $f_{SW}/10$:

  $\omega_C = 2\cdot\pi\cdot f_C$
- Find the mid-band gain A_{VM} to achieve target bandwidth
- Set ω_{ZEA} equal to 1/10 the target crossover frequency:

  $\omega_{ZEA} = \omega_C/10$
- Set ω_{HF} equal to the ESR zero frequency:

  $\omega_{HF} = \omega_Z$

$$G_m(\text{mod}) = \frac{1}{R_i}$$

$$A_{VM} = \frac{\omega_C \cdot C_{OUT}}{G_m(\text{mod})}$$

$$R_{COMP} = A_{VM} \cdot R_{FBT} \text{ (op amp)}$$

$$R_{COMP} = \frac{A_{VM}}{g_m \cdot K_{FB}} \quad (g_m \text{ amp})$$

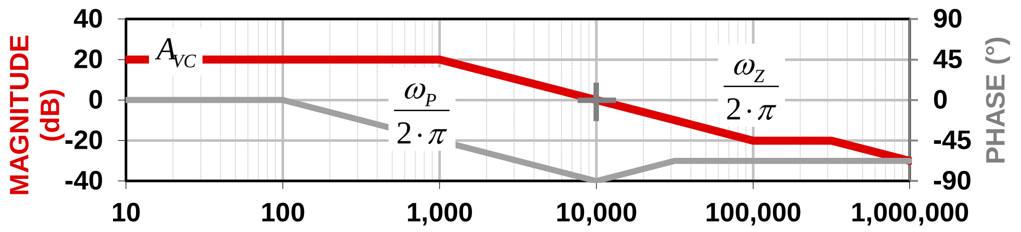
$$C_{COMP} = \frac{1}{\omega_{ZEA} \cdot R_{COMP}}$$

$$C_{HF} = \frac{1}{\omega_{HF} \cdot R_{COMP}}$$

Current-mode buck compensation results

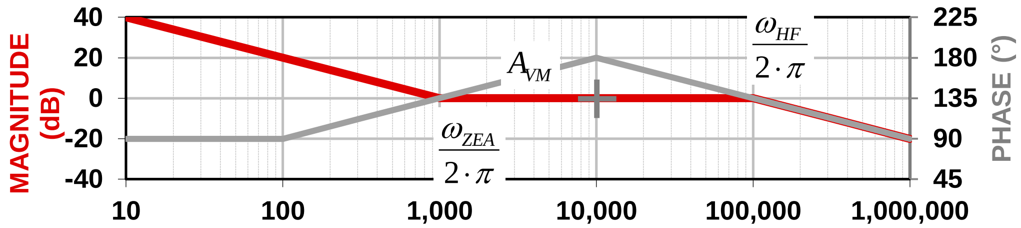
Power stage

$$\frac{\hat{v}_{out}}{\hat{v}_c} \approx A_{VC} \cdot \frac{1+\frac{s}{\omega_z}}{1+\frac{s}{\omega_p}} \cdot F_h(s)$$



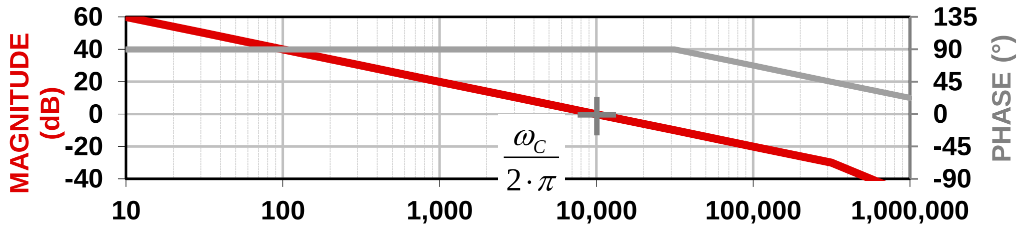
Error amplifier

$$\frac{\hat{v}_C}{\hat{v}'_{OUT}} \approx -A_{VM} \cdot \frac{1+\frac{\omega_{ZEA}}{s}}{1+\frac{s}{\omega_{HF}}}$$



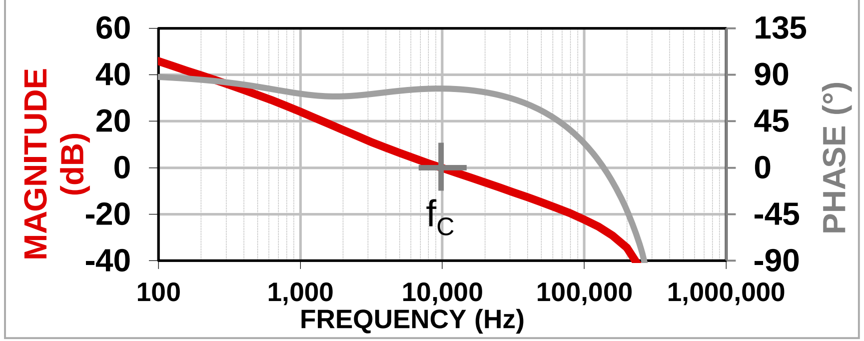
Control loop

$$\frac{\hat{v}_{OUT}}{\hat{v}'_{OUT}} = \frac{\hat{v}_{OUT}}{\hat{v}_C} \cdot \frac{\hat{v}_C}{\hat{v}'_{OUT}}$$

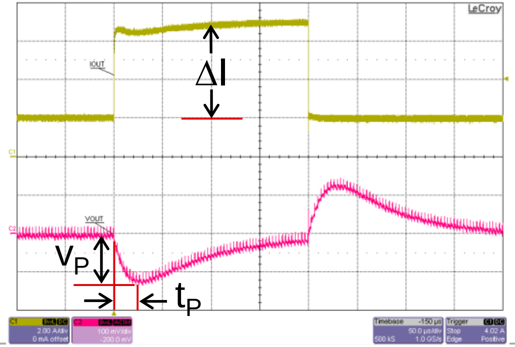


Bandwidth vs transient response

Current-mode bandwidth



Current-mode transient response



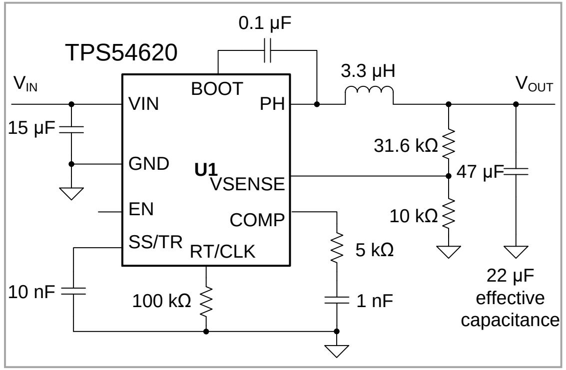
With no ESR, slew rate or duty cycle limiting: $t_P = \frac{1}{4 \cdot f_C}$ $\quad t_P = \frac{1}{4 \cdot 10kHz} = 25\mu s$

Current-mode single pole approximation: $V_P = \frac{\Delta I}{2 \cdot \pi \cdot f_C \cdot C_{OUT}}$ $\quad V_P = \frac{5A}{2 \cdot \pi \cdot 10kHz \cdot 440\mu F} = 180mV$

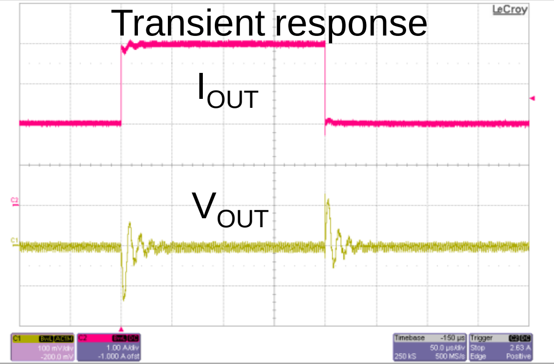
Current-mode critically damped: $V_P = \frac{\Delta I}{e \cdot \pi \cdot f_C \cdot C_{OUT}}$ $\quad V_P = \frac{5A}{e \cdot \pi \cdot 10kHz \cdot 440\mu F} = 130mV$ shown above

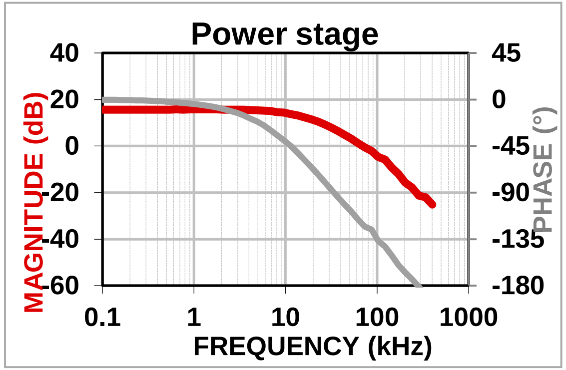
Voltage-mode: $V_P = \frac{\Delta I}{8 \cdot f_C \cdot C_{OUT}}$ $\quad V_P = \frac{5A}{8 \cdot 10kHz \cdot 440\mu F} = 140mV$

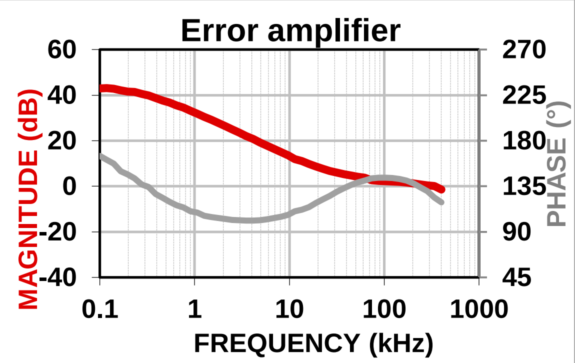
Switching regulator with poor compensation

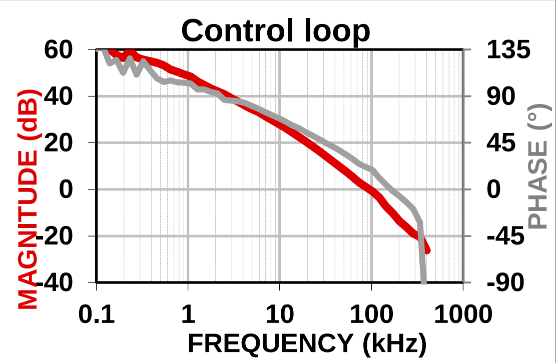


- Power stage: phase at –180° indicates high internal slope compensation
- Error amplifier: zero appears high and mid-band gain is 3 dB
- Control loop: f_C is 95 kHz with only 20° phase margin



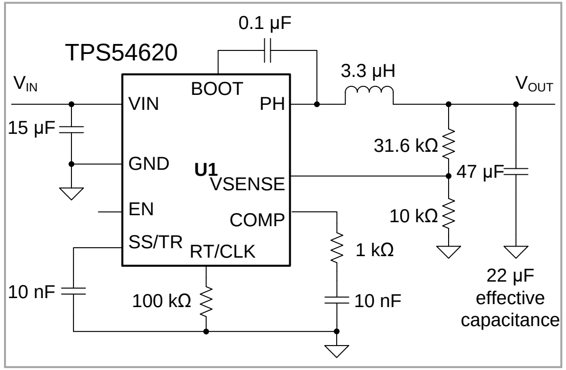




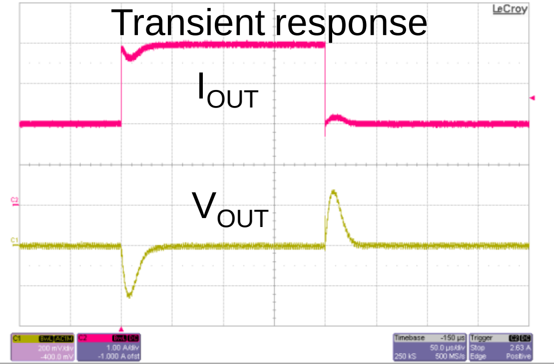


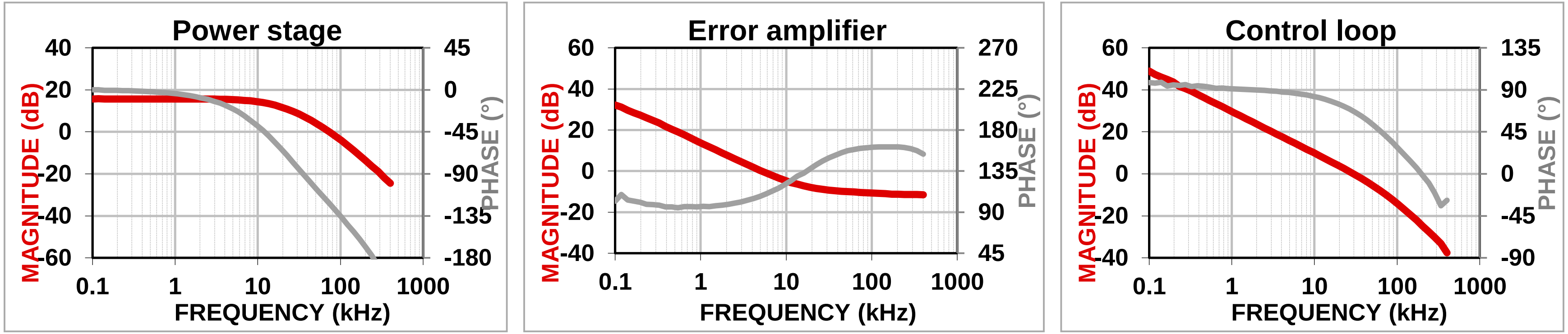
Texas Instruments

Switching regulator with revised compensation



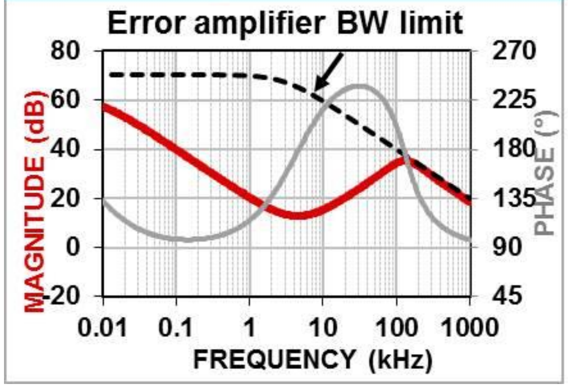
- Power stage: cannot change slope compensation
- Error amplifier: decrease R_{COMP} and rescale C_{COMP}
- Control loop: now f_C is 30 kHz with 67° phase margin





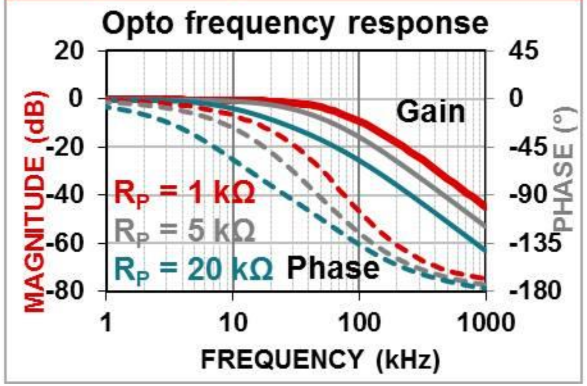
Practical limitations

Error amplifier bandwidth



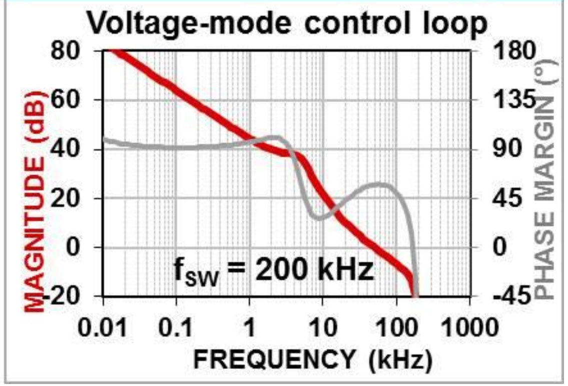
- Error amp BW can limit maximum f_C
- Wider BW op amp needed for voltage-mode due to Type III compensation

Optocoupler bandwidth



- Resistance seen by output transistor forms a pole in kHz range
- More of an issue for forward topologies at higher f_C

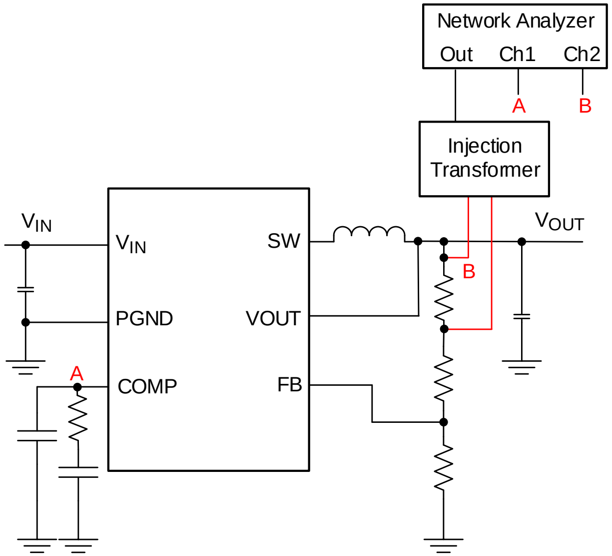
Switching frequency



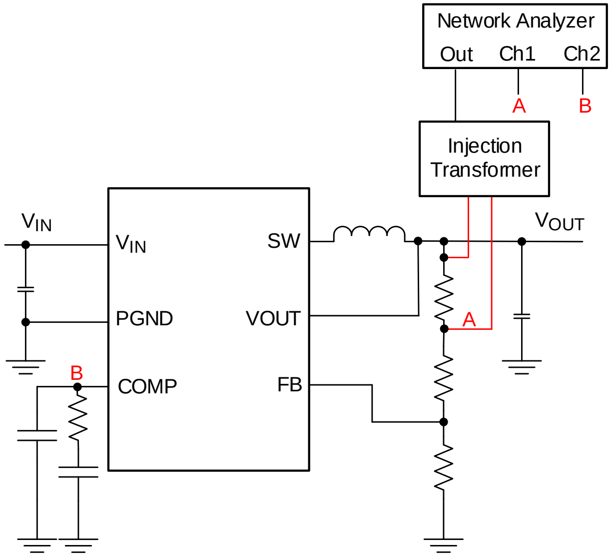
- Maximum f_C is a fraction of f_{SW}
- Rule of thumb is 1/5 to 1/10 of f_{SW}

Measuring transfer functions

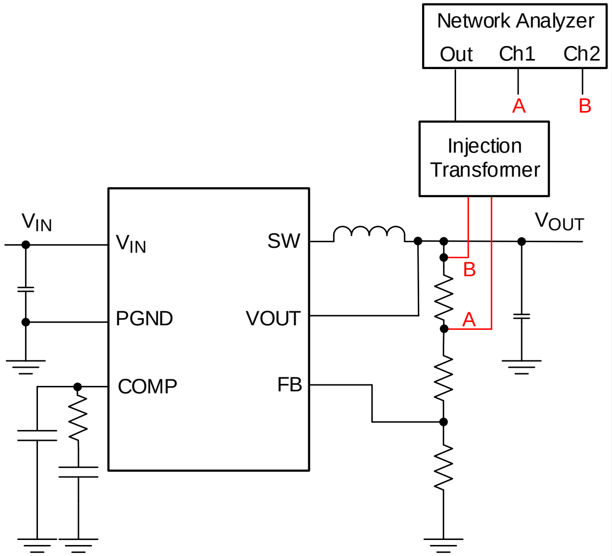
Power stage



Compensator

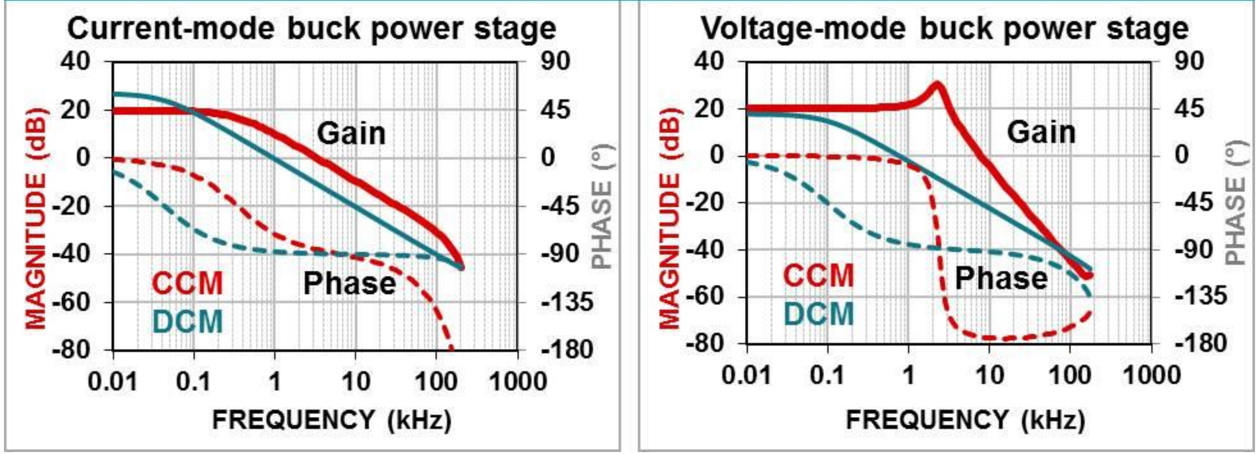


Closed loop



DCM vs CCM characteristics

Discontinuous vs. continuous conduction-mode



- DCM causes a reduction in loop bandwidth compared to CCM
- Generally, if the loop is stable in CCM, it will be stable in DCM

DCM duty cycle

- Buck

$$D = \sqrt{\frac{2 \cdot L \cdot f_{SW} \cdot I_{OUT} \cdot V_{OUT}}{V_{IN} \cdot (V_{IN} - V_{OUT})}}$$

- Boost

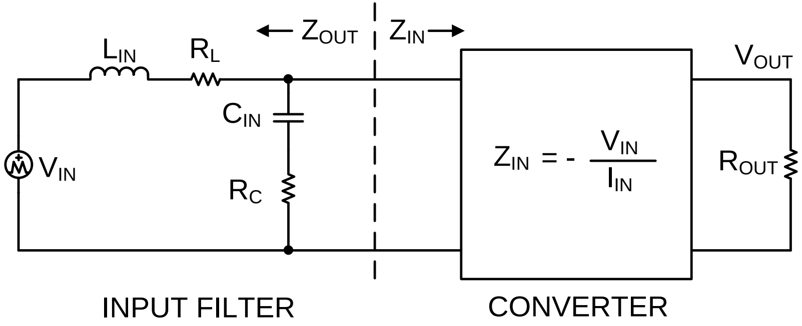
$$D = \frac{\sqrt{2 \cdot L \cdot f_{SW} \cdot I_{OUT} \cdot (V_{OUT} - V_{IN})}}{V_{IN}}$$

- Buck-boost

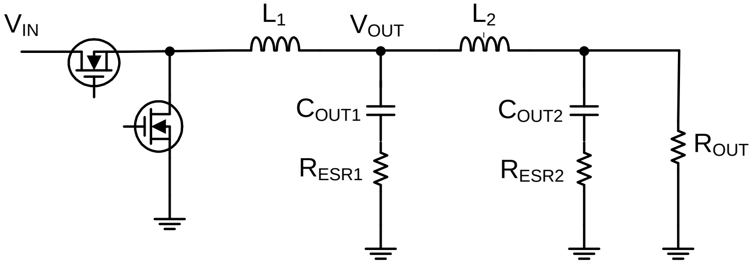
$$D = \frac{\sqrt{2 \cdot L \cdot f_{SW} \cdot I_{OUT} \cdot V_{OUT}}}{V_{IN}}$$

Filter considerations

Input filter stability



Second stage filters



For stability: Filter Z_{OUT} << Converter Z_{IN}

- Characteristic impedance $Z_S = \sqrt{\frac{L_{IN}}{C_{IN}}}$
- Damping factor

$$\zeta = \frac{1}{2} \cdot \left(\frac{R_L + R_C}{Z_S} + \frac{Z_S}{Z_{IN}} \right)$$

- Capacitors: make C_{OUT1} smaller than C_{OUT2}
- Inductors: make L_2 smaller than L_1
- Resonance: make second stage filter resonance 3 times f_C
- Damping: make second stage filter damped to a Q of 1

Summary

- Identify poles and zeros of the power stage
- Select appropriate compensation network based on control mode and topology
- Tune compensation and loop gain to achieve required loop bandwidth and transient response

Resources and references

- "Closing the Feedback Loop" by Lloyd Dixon, SEM300
- "Current-Mode Control of Switching Power Supplies" by Lloyd Dixon, SEM400
- "The Right-Half-Plane Zero -- A Simplified Explanation" by Lloyd Dixon, SEM500
- "Isolating the Control Loop" by Robert Mammano, SEM700
- "Control Loop Design" by Lloyd Dixon, SEM800
- "Control Loop Cookbook" by Lloyd Dixon, SEM1100
- "A New Small-Signal Model for Current-Mode Control" by Ray Ridley
- "Current-Mode Control Modeling" by Ray Ridley
- "Designing Stable Control Loops" by Dan Mitchell and Bob Mammano, SEM1400
- "Current-Mode Modeling – Reference Guide" by Robert Sheehan, SNVA542
- "Understanding and Applying Current-Mode Control Theory" by Robert Sheehan, SNVA555
- "Frequency Compensation and Power Stage Design for Buck Converters to Meet Load Transient Specifications" by S. Bag, R. Sheehan, et al., APEC 2014
- Power Tips: Compensating Isolated Power Supplies by Brian King
- Practical Feedback Loop Analysis for Current-Mode Boost Converter by SW Lee

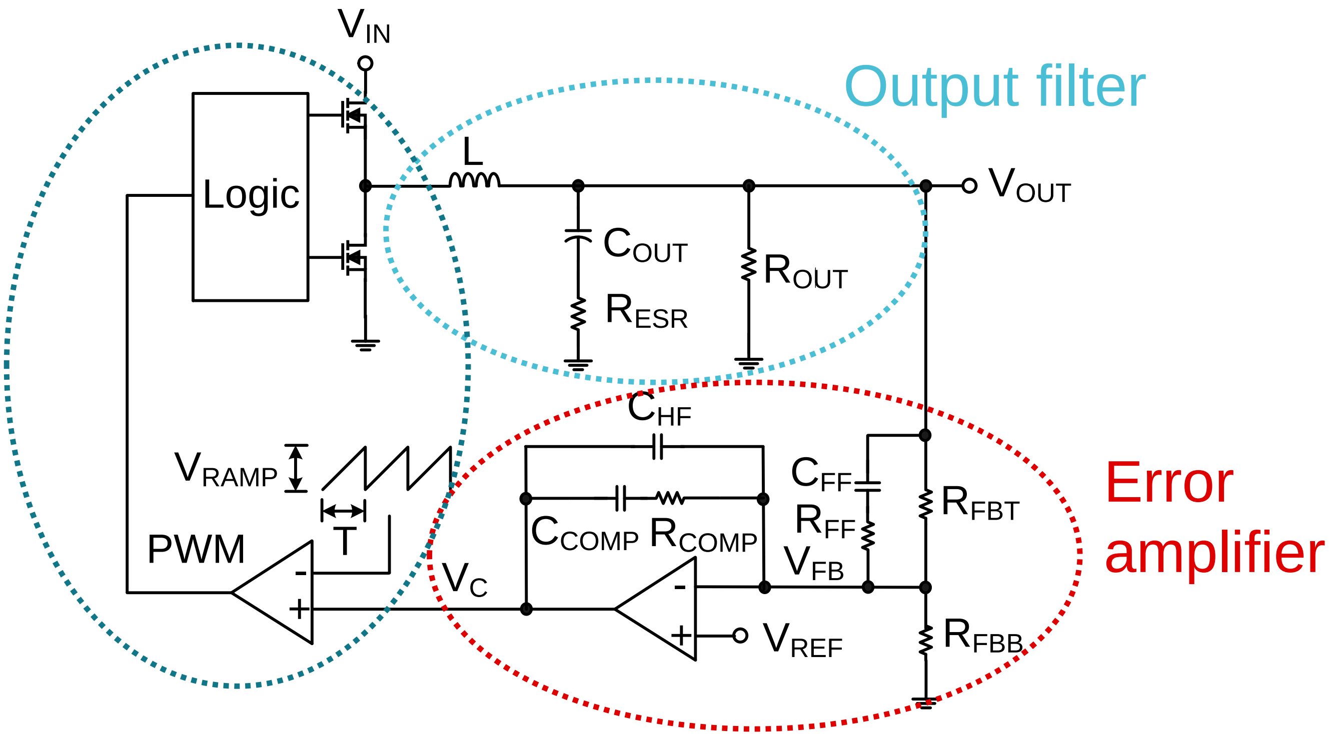
Appendix

Voltage-mode buck

Modulator

$$D = \frac{V_{OUT}}{V_{IN}}$$

$$D' = \frac{V_{IN} - V_{OUT}}{V_{IN}}$$



Voltage-mode buck compensation strategy

- Choose a value for R_{FBT} based on bias current and power dissipation
- Pick target bandwidth, typically $f_{SW}/10$:

  $\omega_C = 2\cdot\pi\cdot f_C$
- Find the mid-band gain A_{VM} to achieve target bandwidth
- Set ω_{ZEA} and ω_{FZ} equal to the output filter complex conjugate pole ω_O:

  $\omega_{ZEA} = \omega_{FZ} = \omega_O$
- Set ω_{FP} equal to the output filter zero ω_Z:

  $\omega_{FP} = \omega_Z$
- Set ω_{HF} equal to half the switching frequency:

  $\omega_{HF} = 2\cdot\pi\cdot f_{SW}/2$

$$A_{VM} = \frac{\omega_C}{A_{VC} \cdot \omega_O}$$

$$R_{COMP} = A_{VM} \cdot R_{FBT}$$

$$C_{COMP} = \frac{1}{\omega_{ZEA} \cdot R_{COMP}}$$

$$C_{FF} = \frac{1}{\omega_{FZ} \cdot R_{FBT}}$$

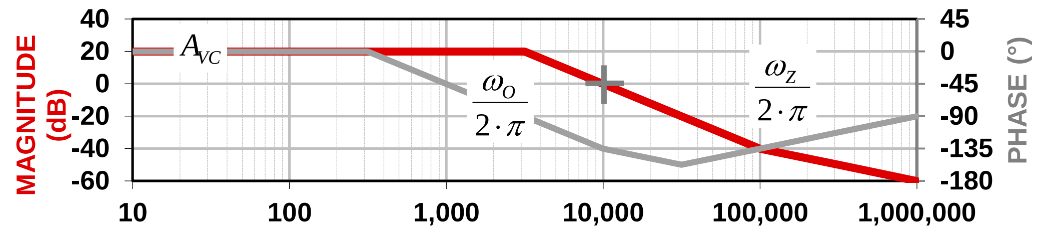
$$R_{FF} = \frac{1}{\omega_{FP} \cdot C_{FF}}$$

$$C_{HF} = \frac{1}{\omega_{HF} \cdot R_{COMP}}$$

Voltage-mode buck compensation results

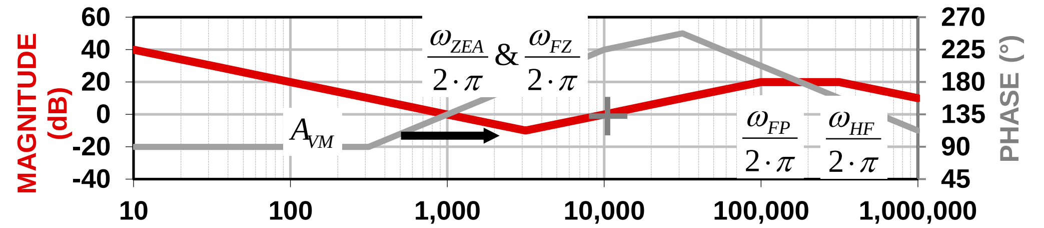
Power stage

$$\frac{\hat{v}_{OUT}}{\hat{v}_C} \approx A_{VC} \cdot \frac{1+\frac{s}{\omega_Z}}{1+\frac{s}{Q_O \cdot \omega_O}+\frac{s^2}{\omega_O^2}}$$



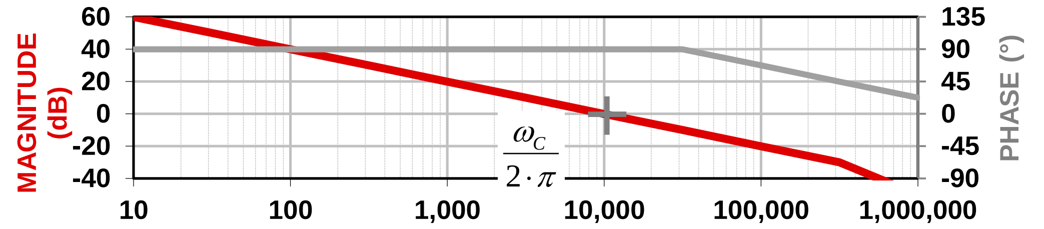
Error amplifier

$$\frac{\hat{v}_C}{\hat{v}'_{OUT}} \approx -A_{VM} \cdot \frac{\left(1+\frac{\omega_{ZEA}}{s}\right)\cdot\left(1+\frac{s}{\omega_{FZ}}\right)}{\left(1+\frac{s}{\omega_{FP}}\right)\cdot\left(1+\frac{s}{\omega_{HF}}\right)}$$

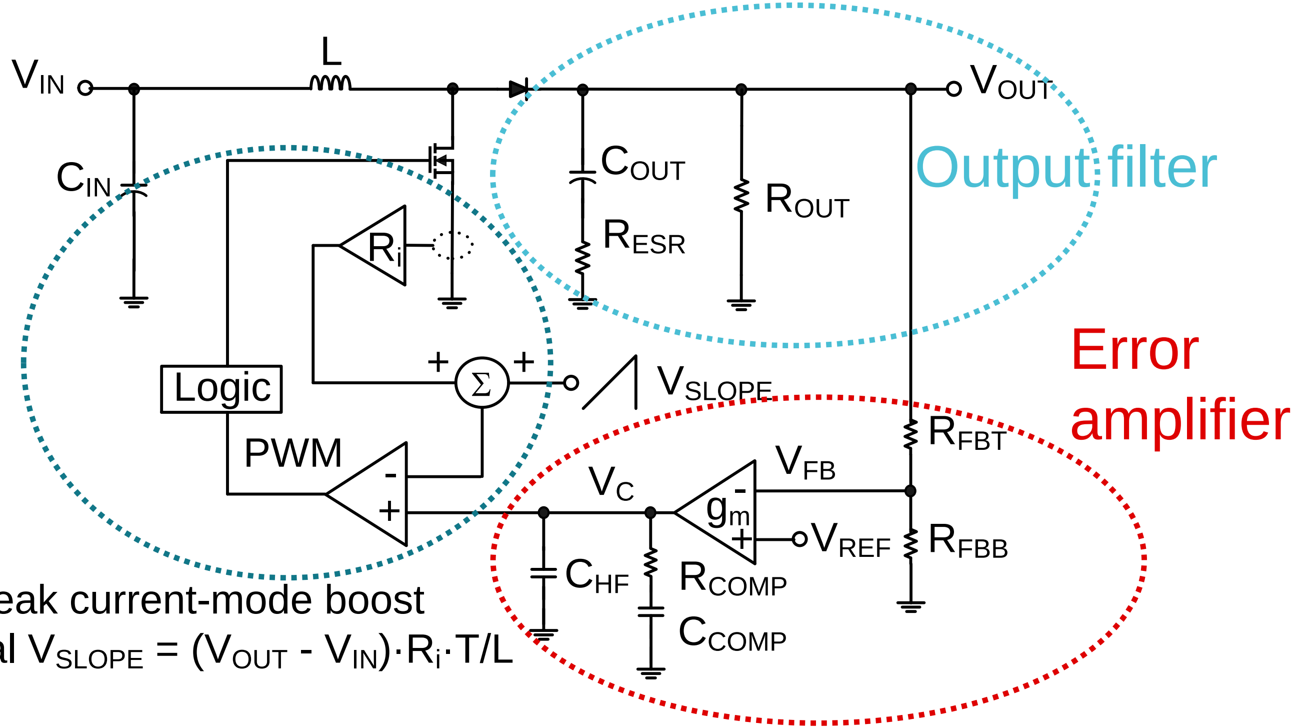


Control loop

$$\frac{\hat{v}_{OUT}}{\hat{v}'_{OUT}} = \frac{\hat{v}_{OUT}}{\hat{v}_C} \cdot \frac{\hat{v}_C}{\hat{v}'_{OUT}}$$



Current-mode boost



$$D = \frac{V_{OUT} - V_{IN}}{V_{OUT}}$$

$$D' = \frac{V_{IN}}{V_{OUT}}$$

Peak current-mode boost

Optimal $V_{SLOPE} = (V_{OUT} - V_{IN}) \cdot R_i \cdot T/L$

Current-mode boost compensation strategy

- Choose a value for R_{FBT} based on bias current and power dissipation
- Find the modulator transconductance in A/V
- Find the RHPZ frequency at minimum input voltage and maximum load current
- Set the target bandwidth to 1/4 of the RHPZ frequency:

  $\omega_C = 2\cdot\pi\cdot f_C = \omega_R/4$
- Find the mid-band gain A_{VM} to achieve target bandwidth
- Set ω_{ZEA} equal to 1/10 the target crossover frequency:

  $\omega_{ZEA} = \omega_C/10$
- Set ω_{HF} equal to the lower of the RHP or ESR zero frequency:

  $\omega_{HF} = \omega_R$ or ω_Z

$$G_m(\text{mod}) = \frac{D'}{R_i}$$

$$\omega_R = \frac{R_{OUT}\cdot D'^2}{L}$$

$$A_{VM} = \frac{\omega_C\cdot C_{OUT}}{G_m(\text{mod})}$$

$$R_{COMP} = A_{VM}\cdot R_{FBT} \text{ (op amp)}$$

$$R_{COMP} = \frac{A_{VM}}{g_m\cdot K_{FB}} \quad (g_m \text{ amp})$$

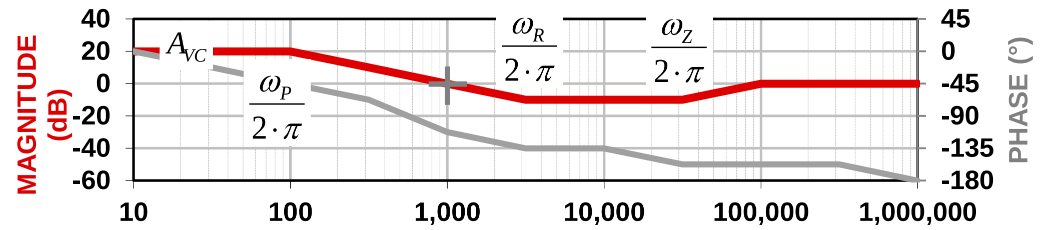
$$C_{COMP} = \frac{1}{\omega_{ZEA}\cdot R_{COMP}}$$

$$C_{HF} = \frac{1}{\omega_{HF}\cdot R_{COMP}}$$

Current-mode boost compensation results

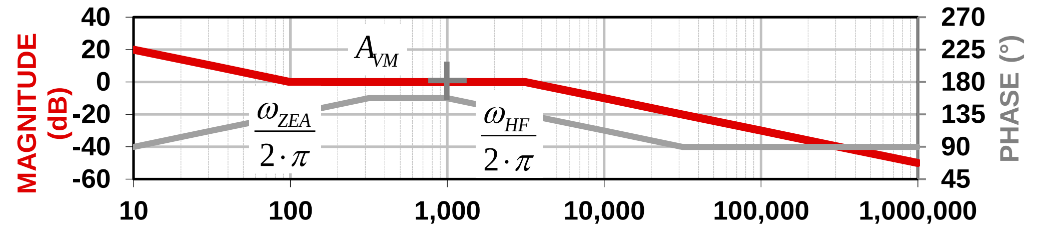
Power stage

$$\frac{\hat{v}_{out}}{\hat{v}_c} \approx A_{VC} \cdot \frac{\left(1+\frac{s}{\omega_z}\right)\left(1-\frac{s}{\omega_r}\right)}{1+\frac{s}{\omega_p}} \cdot F_h(s)$$



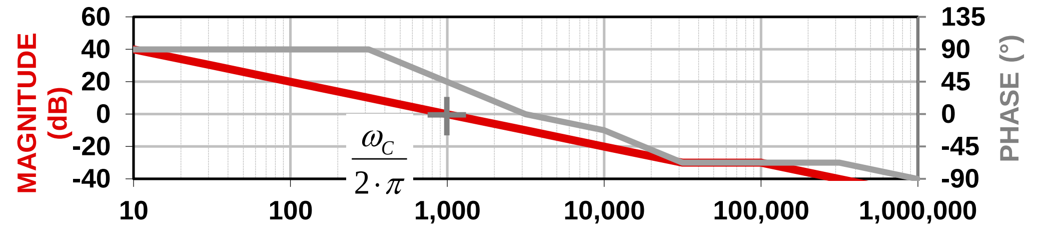
Error amplifier

$$\frac{\hat{v}_C}{\hat{v}'_{OUT}} \approx -A_{VM} \cdot \frac{1+\frac{\omega_{ZEA}}{s}}{1+\frac{s}{\omega_{HF}}}$$



Control loop

$$\frac{\hat{v}_{OUT}}{\hat{v}'_{OUT}} = \frac{\hat{v}_{OUT}}{\hat{v}_C} \cdot \frac{\hat{v}_C}{\hat{v}'_{OUT}}$$

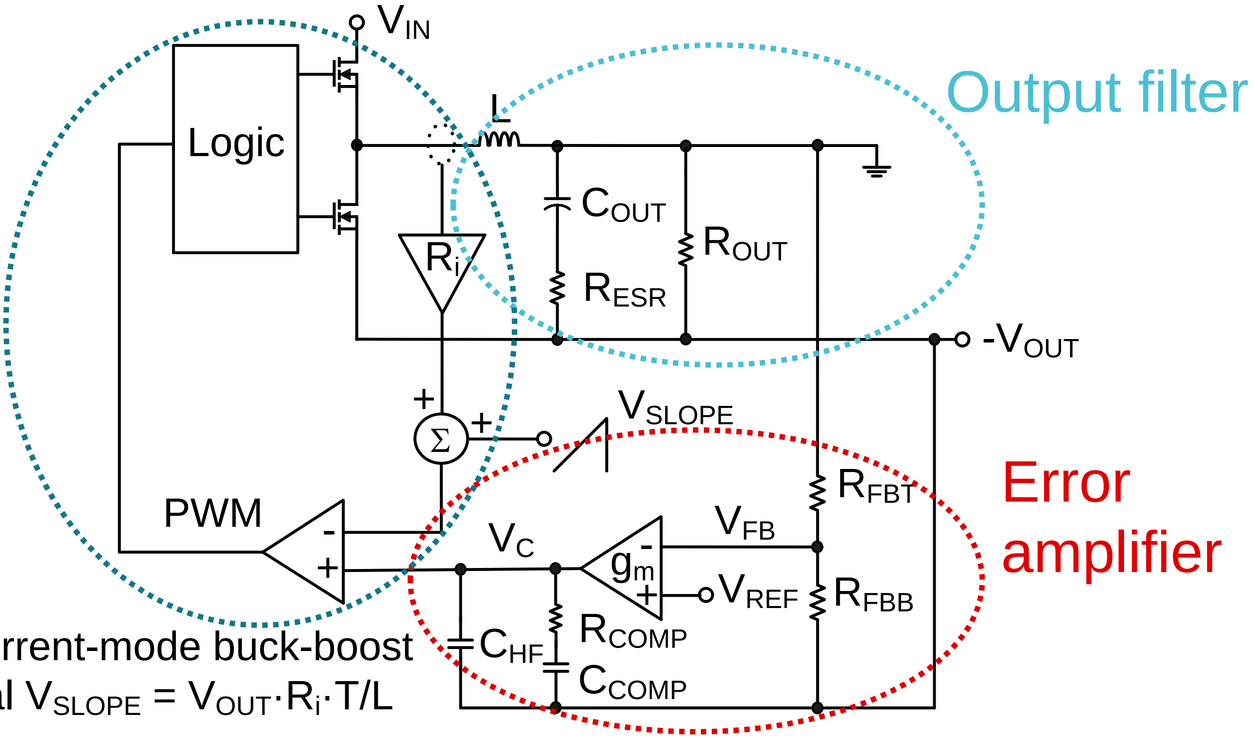


Current-mode buck-boost

Modulator

$$D = \frac{V_{OUT}}{V_{IN} + V_{OUT}}$$

$$D' = \frac{V_{IN}}{V_{IN} + V_{OUT}}$$



Peak current-mode buck-boost
Optimal $V_{SLOPE} = V_{OUT} \cdot R_i \cdot T/L$

Current-mode buck-boost compensation strategy

- Choose a value for R_{FBT} based on bias current and power dissipation
- Find the modulator transconductance in A/V
- Find the RHPZ frequency at minimum input voltage and maximum load current
- Set the target bandwidth to 1/4 of the RHPZ frequency:

  $\omega_C = 2 \cdot \pi \cdot f_C = \omega_R/4$
- Find the mid-band gain A_{VM} to achieve target bandwidth
- Set ω_{ZEA} equal to 1/10 the target crossover frequency:

  $\omega_{ZEA} = \omega_C/10$
- Set ω_{HF} equal to the lower of the RHP or ESR zero frequency:

  $\omega_{HF} = \omega_R$ or ω_Z

$$G_m(\text{mod}) = \frac{D'}{R_i}$$

$$\omega_R = \frac{R_{OUT} \cdot D'^2}{L \cdot D}$$

$$A_{VM} = \frac{\omega_C \cdot C_{OUT}}{G_m(\text{mod})}$$

$$R_{COMP} = A_{VM} \cdot R_{FBT} \text{ (op amp)}$$

$$R_{COMP} = \frac{A_{VM}}{g_m \cdot K_{FB}} \quad (g_m \text{ amp})$$

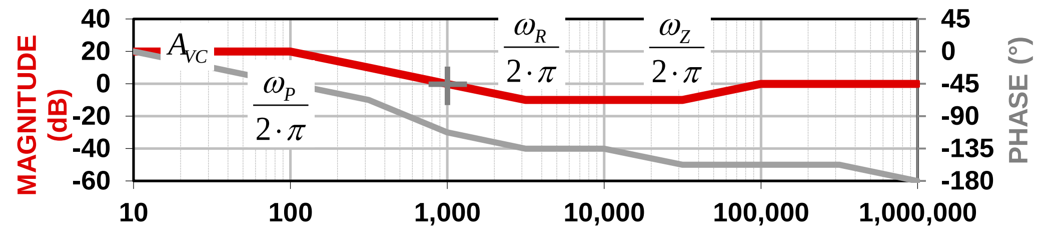
$$C_{COMP} = \frac{1}{\omega_{ZEA} \cdot R_{COMP}}$$

$$C_{HF} = \frac{1}{\omega_{HF} \cdot R_{COMP}}$$

Current-mode buck-boost compensation results

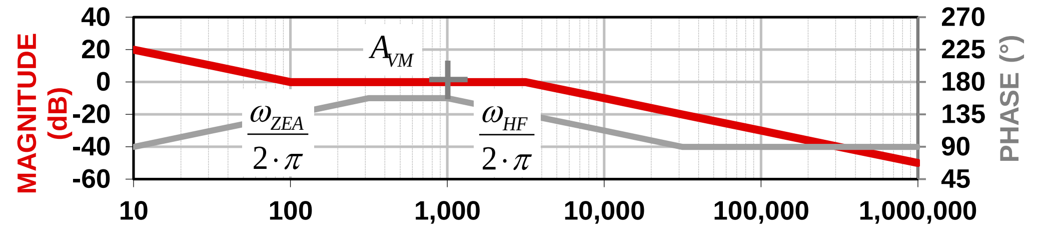
Power stage

$$\frac{\hat{v}_{out}}{\hat{v}_c} \approx A_{VC} \cdot \frac{\left(1+\frac{s}{\omega_z}\right)\left(1-\frac{s}{\omega_r}\right)}{1+\frac{s}{\omega_p}} \cdot F_h(s)$$



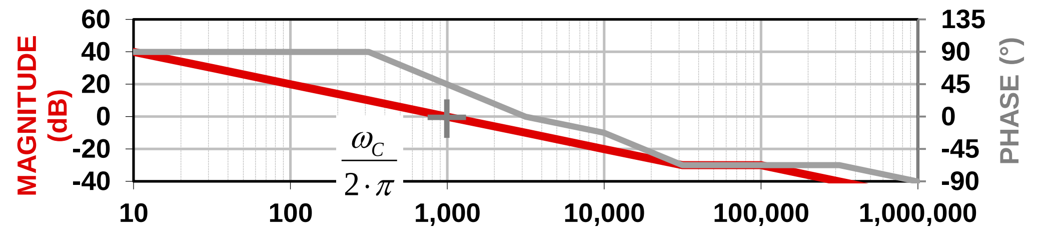
Error amplifier

$$\frac{\hat{v}_C}{\hat{v}'_{OUT}} \approx -A_{VM} \cdot \frac{1+\frac{\omega_{ZEA}}{s}}{1+\frac{s}{\omega_{HF}}}$$

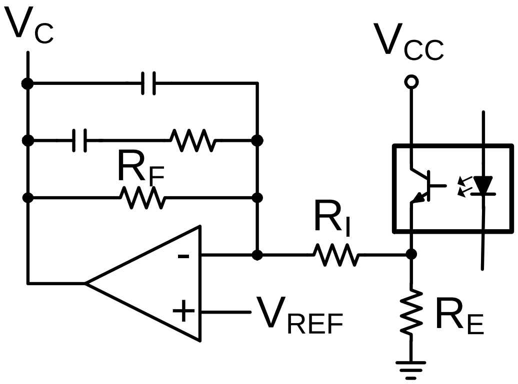
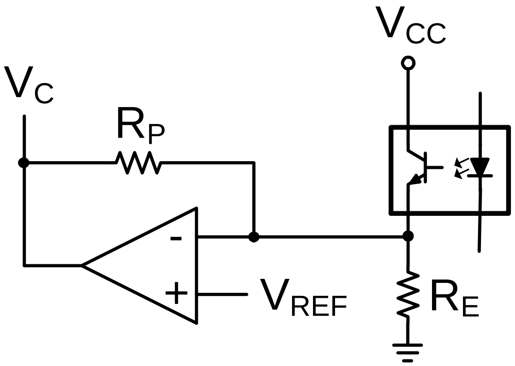


Control loop

$$\frac{\hat{v}_{OUT}}{\hat{v}'_{OUT}} = \frac{\hat{v}_{OUT}}{\hat{v}_C} \cdot \frac{\hat{v}_C}{\hat{v}'_{OUT}}$$

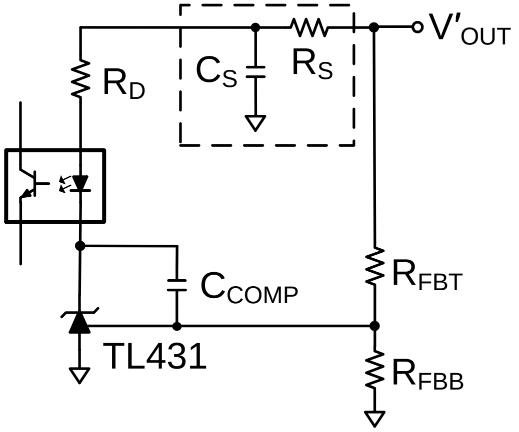


Primary side compensation

Primary side compensation	High bandwidth configuration
	
• Uses primary side inverting amplifier to implement frequency compensation	• Opto emitter is at virtual ground of V_{REF} • This minimizes pole due to opto parasitic capacitance

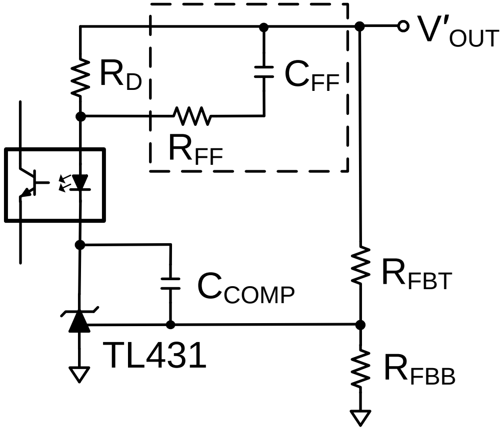
Secondary side compensation

ESR zero compensation



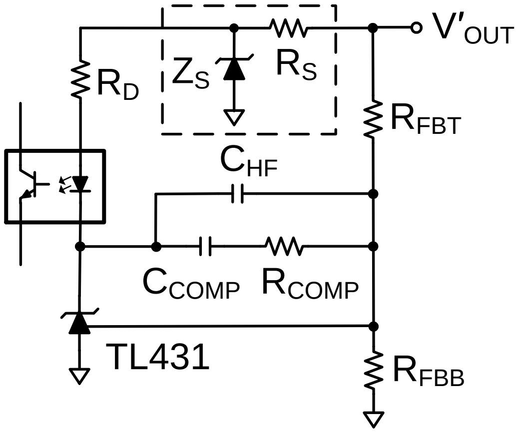
- An RC pole to the opto can be used to cancel the output capacitor ESR zero

Phase boost



- Feed-forward across R_D adds phase boost for increased bandwidth

Zener bias



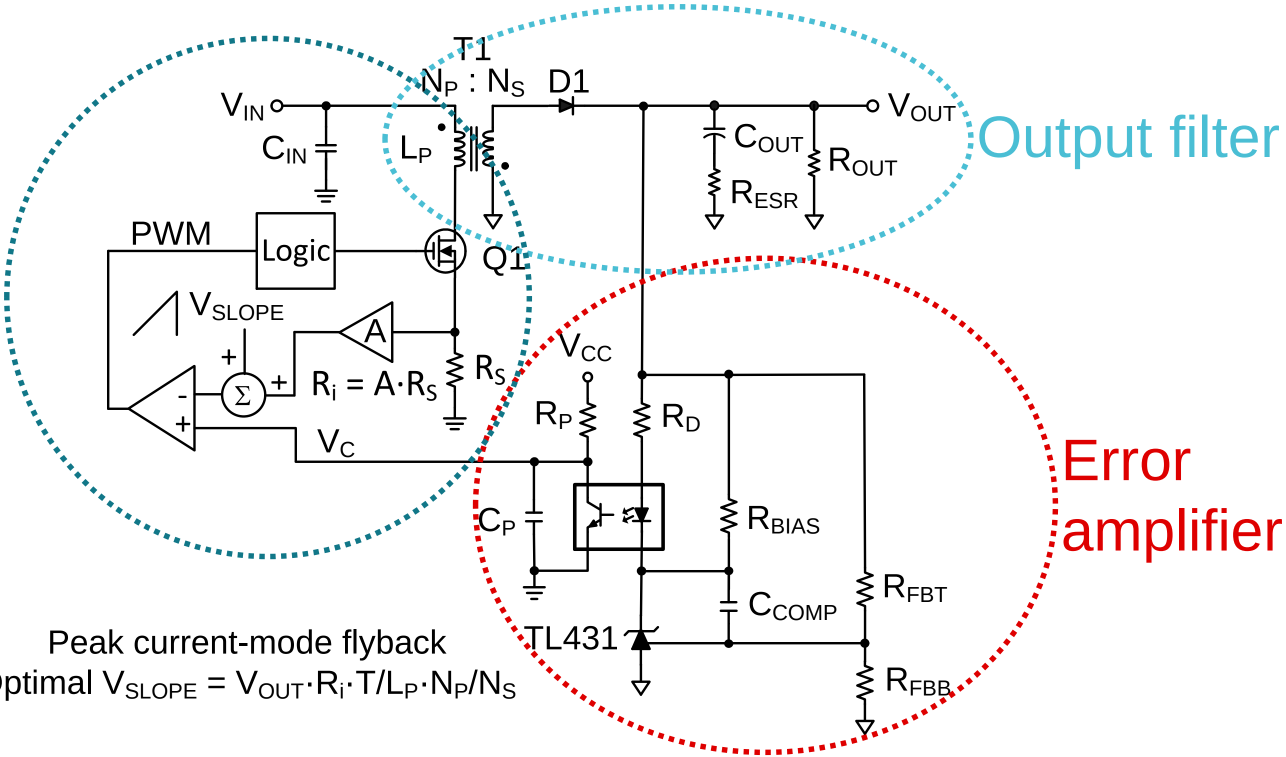
- Zener bias for R_D eliminates the high frequency feedback path for secondary-side compensation

Isolated current-mode flyback

Modulator

$$D = \frac{V_{OUT}}{V_{IN} \cdot \frac{N_S}{N_P} + V_{OUT}}$$

$$D' = \frac{V_{IN}}{V_{IN} + V_{OUT} \cdot \frac{N_P}{N_S}}$$



Peak current-mode flyback

Optimal $V_{SLOPE} = V_{OUT} \cdot R_i \cdot T / L_P \cdot N_P / N_S$

Current-mode flyback compensation strategy

- Choose a value for R_{FBT} based on bias current and power dissipation
- Find the modulator transconductance in A/V
- Find the RHPZ frequency at minimum input voltage and maximum load current
- Set the target bandwidth to 1/4 of the RHPZ frequency:
  $\omega_C = 2 \cdot \pi \cdot f_C = \omega_R/4$
- Find the mid-band gain A_{VM} to achieve target bandwidth
  Adjust R_D, R_P and C_{OUT} as required
- Set ω_{ZEA} equal to 1/10 the target crossover frequency:
  $\omega_{ZEA} = \omega_C/10$
- Set ω_{HF} equal to the lower of the RHP or ESR zero frequency:
  $\omega_{HF} = \omega_R$ or ω_Z

$$G_m(\text{mod}) = \frac{D'}{R_i} \cdot \frac{N_P}{N_S}$$

$$\omega_R = \frac{R_{OUT} \cdot D'^2}{L_P \cdot D} \cdot \left(\frac{N_P}{N_S}\right)^2$$

$$A_{VM} = \frac{\omega_C \cdot C_{OUT}}{G_m(\text{mod})}$$

$$R_D = CTR \cdot \frac{R_P}{\text{A}_{\text{VM}}}$$

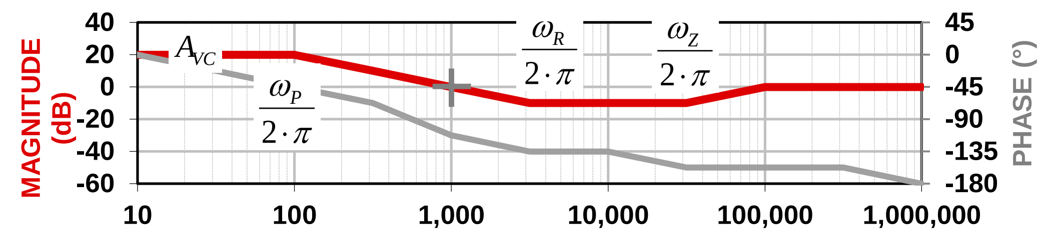
$$C_{COMP} = \frac{1}{R_{FBT} \cdot \omega_{ZEA}}$$

$$C_P = \frac{1}{R_P \cdot \omega_{HF}}$$

Current-mode flyback compensation results

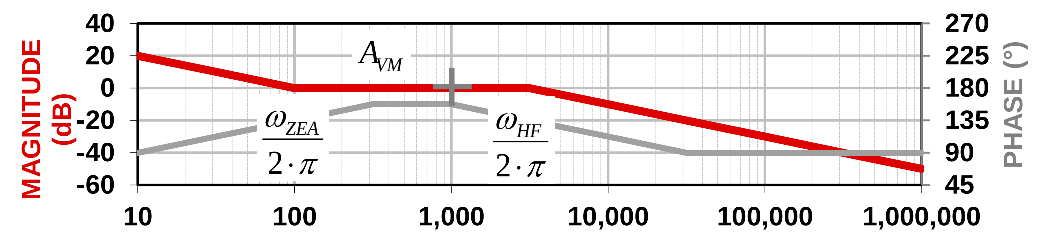
Power stage

$$\frac{\hat{v}_{out}}{\hat{v}_c} \approx A_{VC} \cdot \frac{\left(1+\frac{s}{\omega_z}\right)\left(1-\frac{s}{\omega_r}\right)}{1+\frac{s}{\omega_p}} \cdot F_h(s)$$



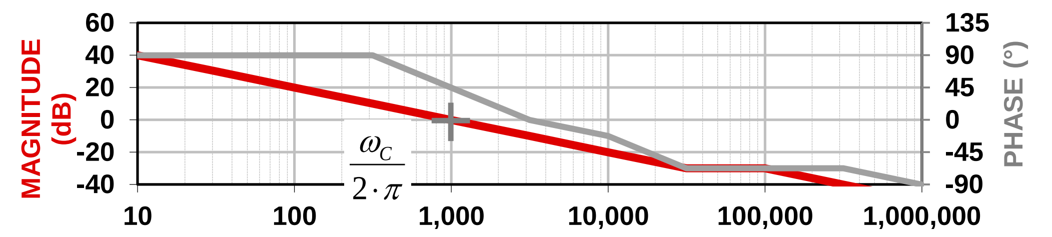
Error amplifier

$$\frac{\hat{v}_C}{\hat{v}'_{OUT}} \approx -A_{VM} \cdot \frac{1+\frac{\omega_{ZEA}}{s}}{1+\frac{s}{\omega_{HF}}}$$



Control loop

$$\frac{\hat{v}_{OUT}}{\hat{v}'_{OUT}} = \frac{\hat{v}_{OUT}}{\hat{v}_C} \cdot \frac{\hat{v}_C}{\hat{v}'_{OUT}}$$



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