

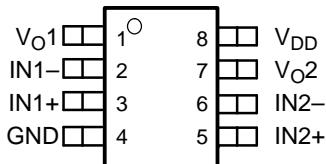


150-mW STEREO AUDIO POWER AMPLIFIER

FEATURES

- 150-mW Stereo Output
- Wide Range of Supply Voltages
 - Fully Specified for 3.3-V and 5-V Operation
 - Operational From 2.5 V to 5.5 V
- Thermal and Short-Circuit Protection
- Surface-Mount Packaging
 - PowerPAD™ MSOP
 - SOIC
- Standard Operational Amplifier Pinout

D OR DGN PACKAGE
(TOP VIEW)

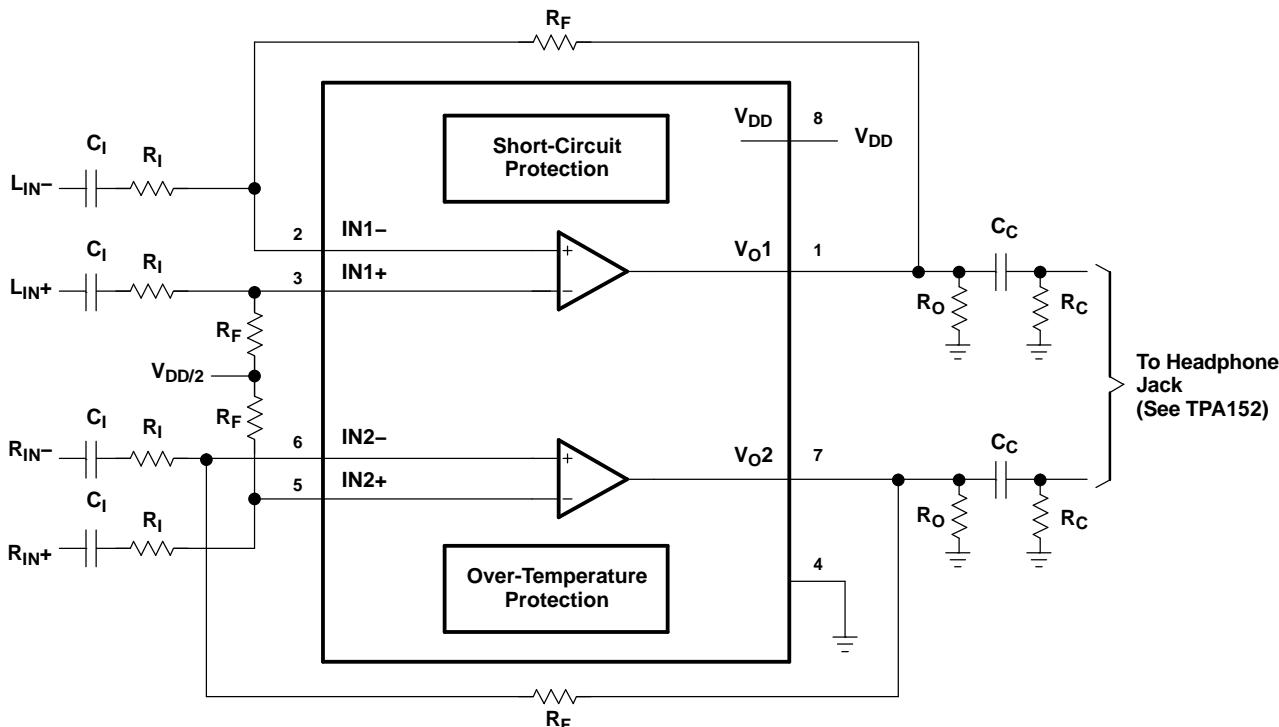


DESCRIPTION

The TPA112 is a stereo audio power amplifier packaged in an 8-pin PowerPAD™ MSOP package capable of delivering 150 mW of continuous RMS power per channel into 8- Ω loads. Amplifier gain is externally configured by means of two resistors per input channel and does not require external compensation for settings of 1 to 10.

THD+N when driving an 8- Ω load from 5 V is 0.1% at 1 kHz, and less than 2% across the audio band of 20 Hz to 20 kHz. For 32- Ω loads, the THD+N is reduced to less than 0.06% at 1 kHz, and is less than 1% across the audio band of 20 Hz to 20 kHz. For 10-k Ω loads, the THD+N performance is 0.01% at 1 kHz, and less than 0.02% across the audio band of 20 Hz to 20 kHz.

FUNCTIONAL BLOCK DIAGRAM



Please be aware that an important notice concerning availability, standard warranty, and use in critical applications of Texas Instruments semiconductor products and disclaimers thereto appears at the end of this data sheet.

PowerPAD is a trademark of Texas Instruments.



These devices have limited built-in ESD protection. The leads should be shorted together or the device placed in conductive foam during storage or handling to prevent electrostatic damage to the MOS gates.

AVAILABLE OPTIONS

T _A	PACKAGED DEVICES		MSOP SYMBOLIZATION
	SMALL OUTLINE ⁽¹⁾ (D)	MSOP ⁽¹⁾ (DGN)	
−40°C to 85°C	TPA112D	TPA112DGN	TI AAD

(1) The D and DGN packages are available in lead-ended tape and reel only (e.g., TPA112DR, TPA112DGNR).

Terminal Functions

TERMINAL NAME NO.	I/O	DESCRIPTION
GND 4	I	GND is the ground connection.
IN1- 2	I	IN1- is the inverting input for channel 1.
IN1+ 3	I	IN1+ is the noninverting input for channel 1.
IN2- 6	I	IN2- is the inverting input for channel 2.
IN2+ 5	I	IN2+ is the noninverting input for channel 2.
V _{DD} 8	I	V _{DD} is the supply voltage terminal.
V _O 1 1	O	V _O 1 is the audio output for channel 1.
V _O 2 7	O	V _O 2 is the audio output for channel 2.

ABSOLUTE MAXIMUM RATINGS

over operating free-air temperature range (unless otherwise noted)⁽¹⁾

		UNIT
V _{DD}	Supply voltage	6 V
V _I	Differential input voltage	−0.3 V to V _{DD} + 0.3 V
I _I	Input current	±2.5 μA
I _O	Output current	±250 mA
	Continuous total power dissipation	Internally limited
T _J	Operating junction temperature range	−40°C to 150°C
T _{stg}	Storage temperature range	−65°C to 150°C
	Lead temperature 1.6 mm (1/16 inch) from case for 10 seconds	260°C

(1) Stresses beyond those listed under "absolute maximum ratings" may cause permanent damage to the device. These are stress ratings only, and functional operation of the device at these or any other conditions beyond those indicated under "recommended operating conditions" is not implied. Exposure to absolute-maximum-rated conditions for extended periods may affect device reliability.

DISSIPATION RATING TABLE

PACKAGE	T _A ≤ 25°C POWER RATING	DERATING FACTOR ABOVE T _A = 25°C	T _A = 70°C POWER RATING	T _A = 85°C POWER RATING
D	725 mW	5.8 mW/°C	464 mW	377 mW
DGN	2.14 W ⁽¹⁾	17.1 mW/°C	1.37 W	1.11 W

(1) See the Texas Instruments document, *PowerPAD Thermally Enhanced Package Application Report* (SLMA002), for more information on the PowerPAD package. The thermal data was measured on a PCB layout based on the information in the section entitled *Texas Instruments Recommended Board for PowerPAD*, of that document.

RECOMMENDED OPERATING CONDITIONS

		MIN	MAX	UNIT
V_{DD}	Supply voltage	2.5	5.5	V
T_A	Operating free-air temperature	-40	85	°C

DC ELECTRICAL CHARACTERISTICS

 at $T_A = 25^\circ\text{C}$, $V_{DD} = 3.3\text{ V}$

PARAMETER	TEST CONDITIONS	MIN	TYP	MAX	UNIT
V_{OO}			10		mV
PSRR	$V_{DD} = 3.2\text{ V to }3.4\text{ V}$	83			dB
$I_{DD(q)}$		1.5	3		mA
Z_I			> 1		MΩ

AC OPERATING CHARACTERISTICS
 $V_{DD} = 3.3\text{ V}$, $T_A = 25^\circ\text{C}$, $R_L = 8\text{ }\Omega$

PARAMETER	TEST CONDITIONS	MIN	TYP	MAX	UNIT
P_O	THD ≤ 0.1%	70 ⁽¹⁾			mW
THD+N	$P_O = 70\text{ mW}$, 20 Hz–20 kHz	2%			
B_{OM}	$G = 10$, THD < 5%	> 20			kHz
Phase margin	Open loop	58°			
S_{VRR}	$f = 1\text{ kHz}$	68			dB
Channel/channel output separation	$f = 1\text{ kHz}$	86			dB
SNR	$P_O = 100\text{ mW}$	100			dB
V_n		9.5			µV(rms)

(1) Measured at 1 kHz

DC ELECTRICAL CHARACTERISTICS

 at $T_A = 25^\circ\text{C}$, $V_{DD} = 5\text{ V}$

PARAMETER	TEST CONDITIONS	MIN	TYP	MAX	UNIT
V_{OO}			10		mV
PSRR	$V_{DD} = 4.9\text{ V to }5.1\text{ V}$	76			dB
$I_{DD(q)}$		1.5	3		mA
Z_I			> 1		MΩ

AC OPERATING CHARACTERISTICS
 $V_{DD} = 5\text{ V}$, $T_A = 25^\circ\text{C}$, $R_L = 8\text{ }\Omega$

PARAMETER	TEST CONDITIONS	MIN	TYP	MAX	UNIT
P_O	THD ≤ 0.1%	70 ⁽¹⁾			mW
THD+N	$P_O = 150\text{ mW}$, 20 Hz–20 kHz	2%			
B_{OM}	$G = 10$, THD < 5%	> 20			kHz
Phase margin	Open loop	56°			
S_{VRR}	$f = 1\text{ kHz}$	68			dB
Channel/channel output separation	$f = 1\text{ kHz}$	86			dB
SNR	$P_O = 150\text{ mW}$	100			dB
V_n		9.5			µV(rms)

(1) Measured at 1 kHz

AC OPERATING CHARACTERISTICS

$V_{DD} = 3.3$ V, $T_A = 25^\circ\text{C}$, $R_L = 32 \Omega$

PARAMETER	TEST CONDITIONS	MIN	TYP	MAX	UNIT
P_O Output power (each channel)	THD $\leq 0.1\%$	40 ⁽¹⁾			mW
THD+N Total harmonic distortion + noise	$P_O = 30$ mW, 20 Hz–20 kHz	0.5%			
B_{OM} Maximum output power BW	$G = 10$, THD $< 2\%$	> 20			kHz
Phase margin	Open loop	58°			
S_{VRR} Supply ripple rejection	$f = 1$ kHz	68			dB
Channel/channel output separation	$f = 1$ kHz	86			dB
SNR Signal-to-noise ratio	$P_O = 100$ mW	100			dB
V_n Noise output voltage		9.5			µV(rms)

(1) Measured at 1 kHz

AC OPERATING CHARACTERISTICS

$V_{DD} = 5$ V, $T_A = 25^\circ\text{C}$, $R_L = 32 \Omega$

PARAMETER	TEST CONDITIONS	MIN	TYP	MAX	UNIT
P_O Output power (each channel)	THD $\leq 0.1\%$	40 ⁽¹⁾			mW
THD+N Total harmonic distortion + noise	$P_O = 60$ mW, 20 Hz–20 kHz	0.4%			
B_{OM} Maximum output power BW	$G = 10$, THD $< 2\%$	> 20			kHz
Phase margin	Open loop	56°			
S_{VRR} Supply ripple rejection	$f = 1$ kHz	68			dB
Channel/channel output separation	$f = 1$ kHz	86			dB
SNR Signal-to-noise ratio	$P_O = 150$ mW	100			dB
V_n Noise output voltage		9.5			µV(rms)

(1) Measured at 1 kHz

TYPICAL CHARACTERISTICS

Table of Graphs

			FIGURE
THD+N	Total harmonic distortion plus noise	vs Frequency	1, 2, 4, 5, 7, 8, 10, 11, 13, 14, 16, 17, 34, 36
		vs Output power	3, 6, 9, 12, 15, 18
PSSR	Power supply rejection ratio	vs Frequency	19, 20
V_n	Output noise voltage	vs Frequency	21, 22
	Crosstalk	vs Frequency	23-26, 37, 38
	Mute attenuation	vs Frequency	27, 28
	Open-loop gain	vs Frequency	29, 30
	Phase margin	vs Frequency	29, 30
	Phase	vs Frequency	39-44
	Output power	vs Load resistance	31, 32
I_{CC}	Supply current	vs Supply voltage	33
SNR	Signal-to-noise ratio	vs Voltage gain	35
	Closed-loop gain	vs Frequency	39-44
	Power dissipation/amplifier	vs Output power	45, 46

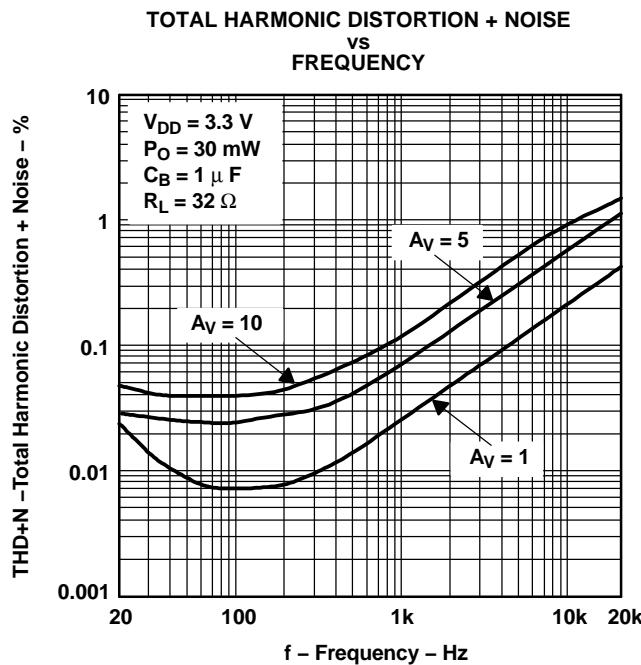


Figure 1.

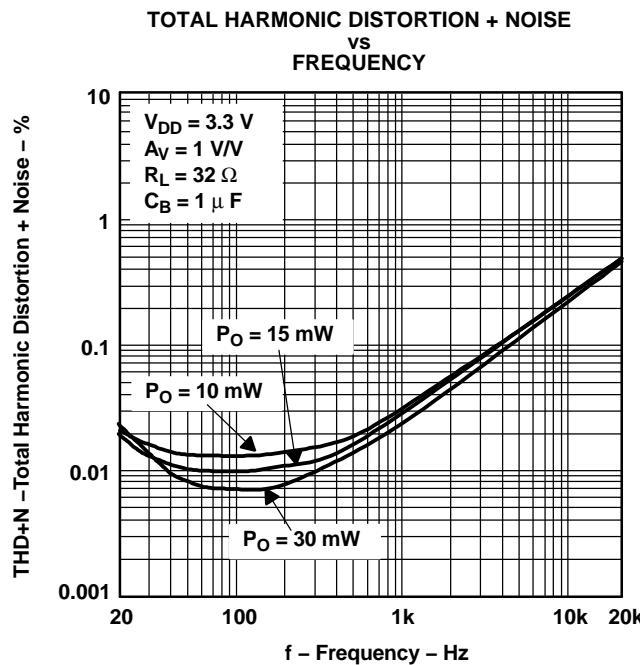


Figure 2.

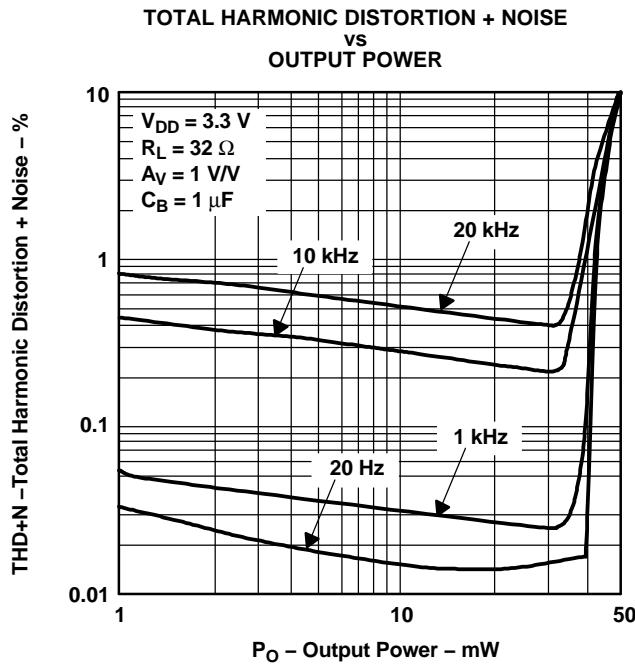


Figure 3.

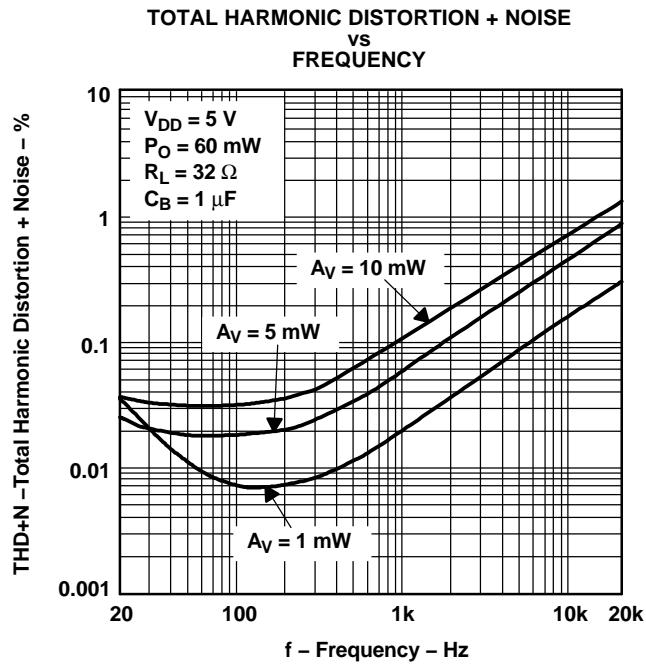


Figure 4.

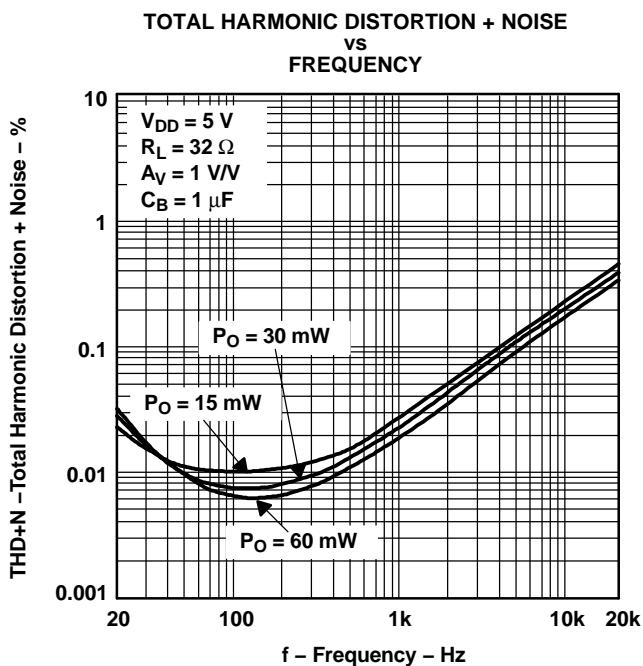


Figure 5.

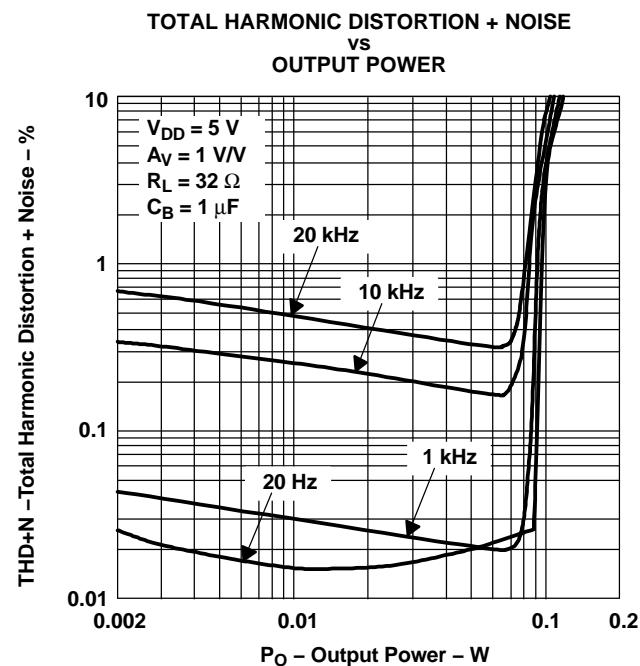


Figure 6.

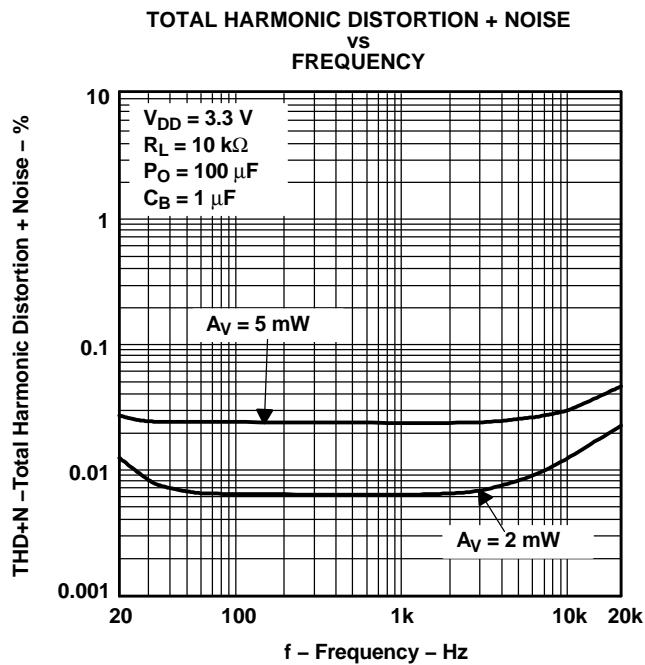


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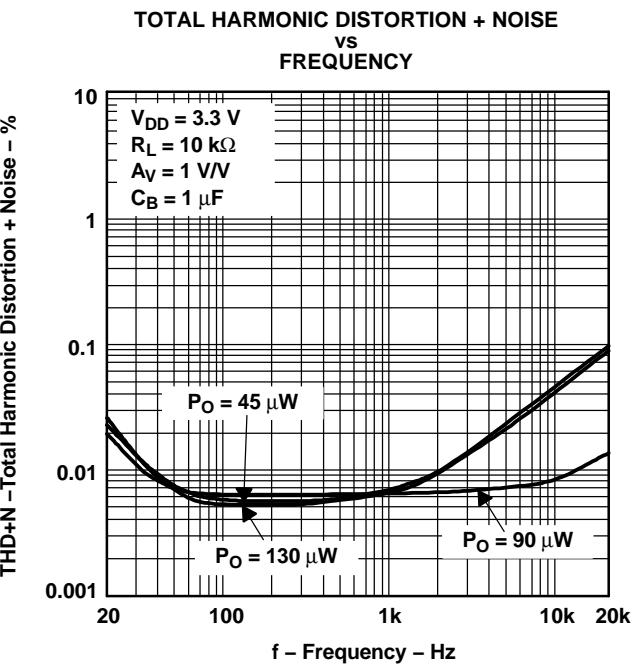


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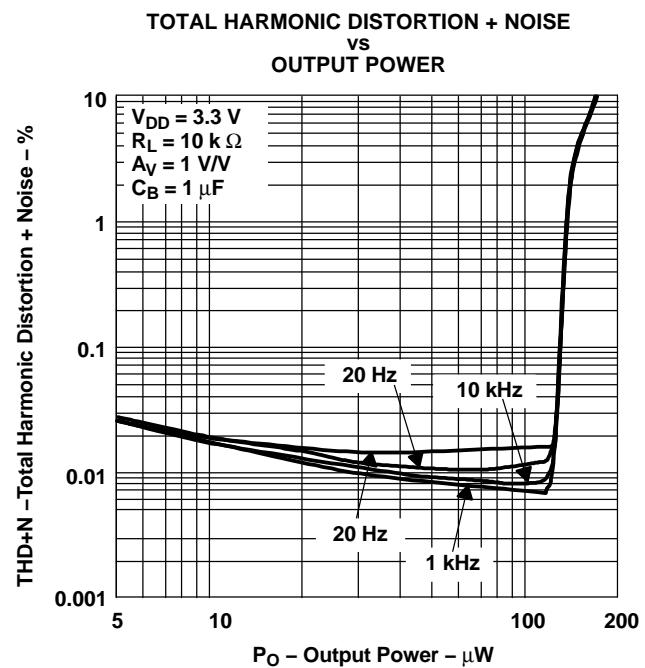


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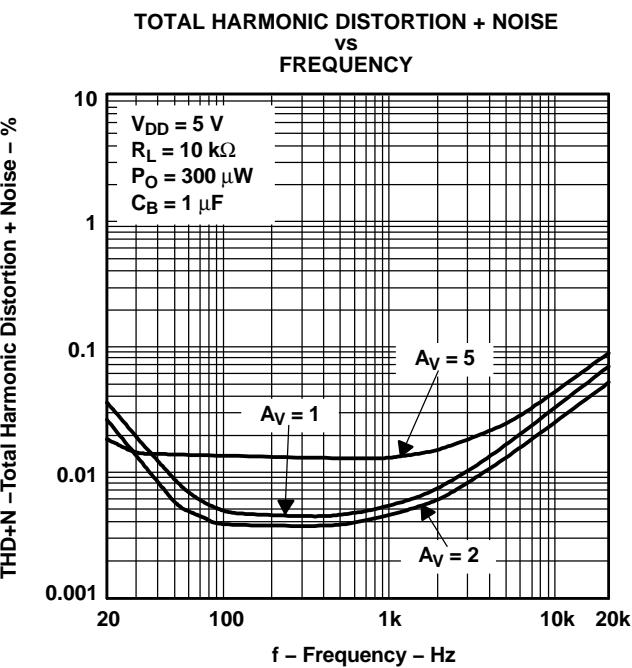


Figure 10.

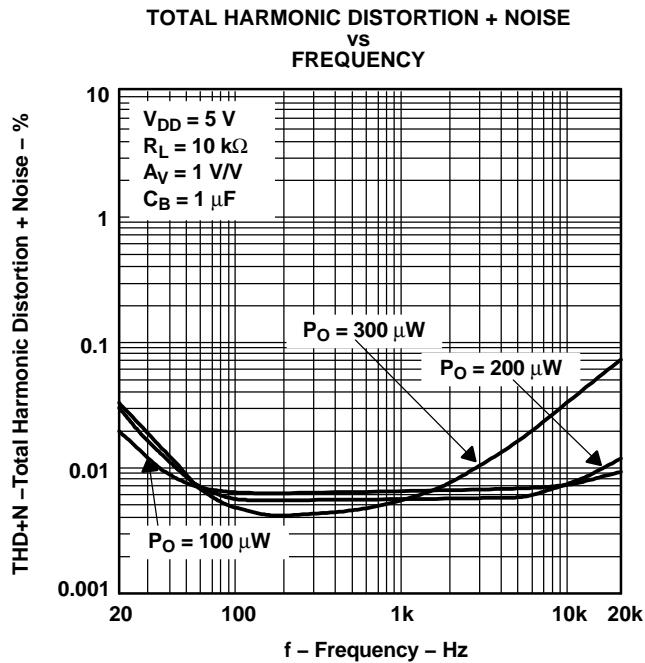


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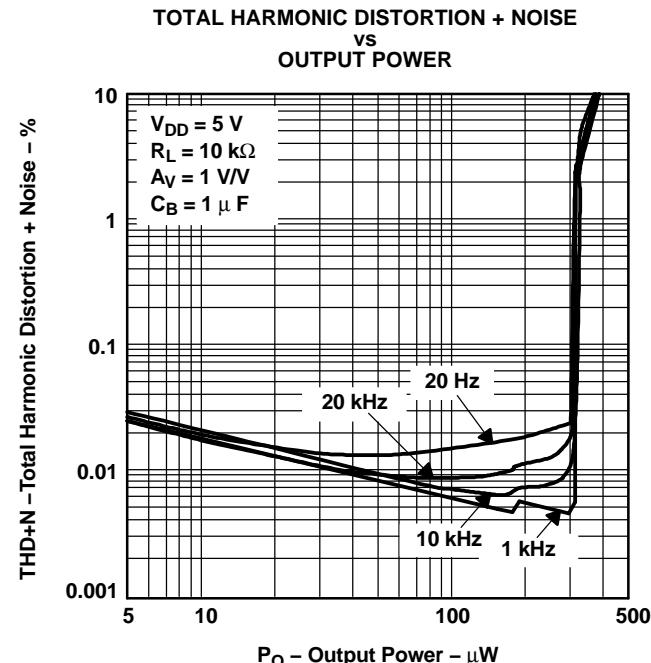


Figure 12.

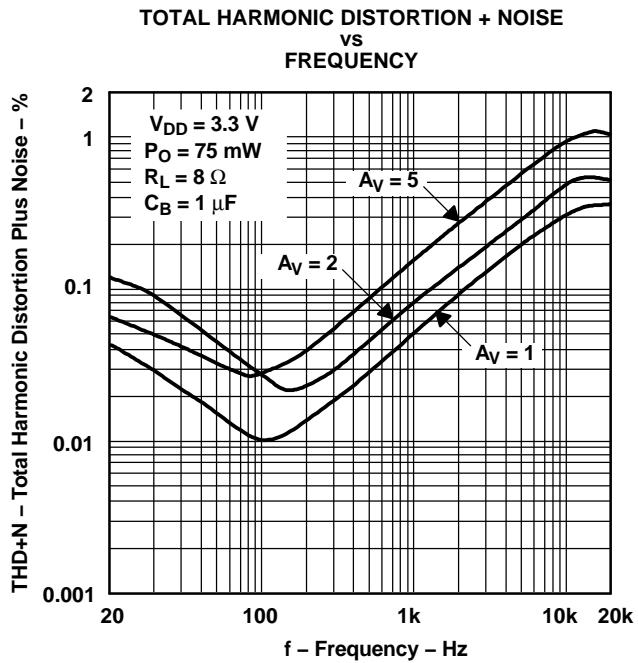


Figure 13.

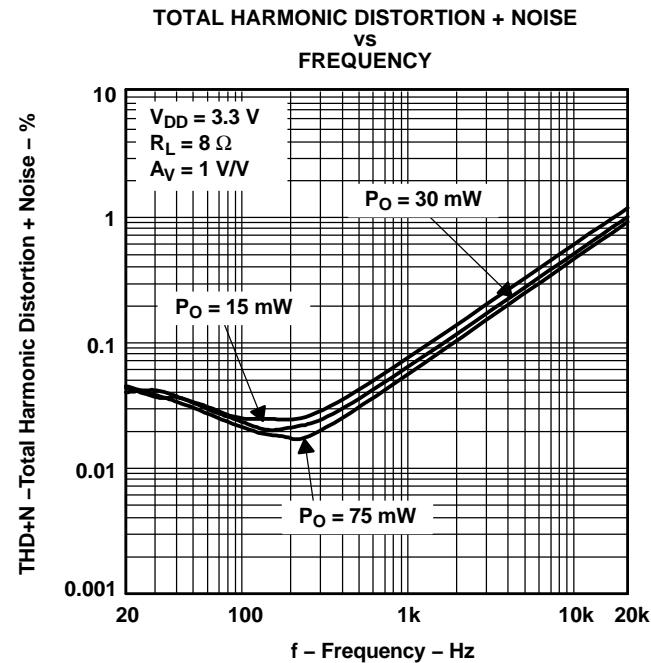


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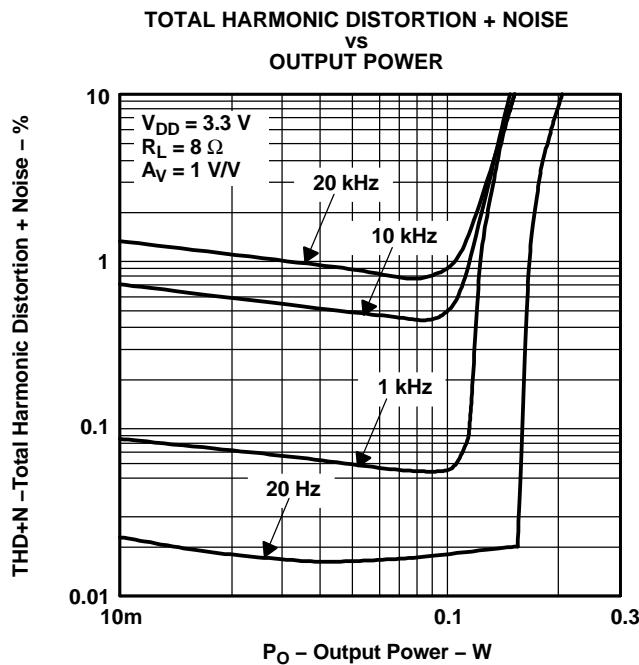


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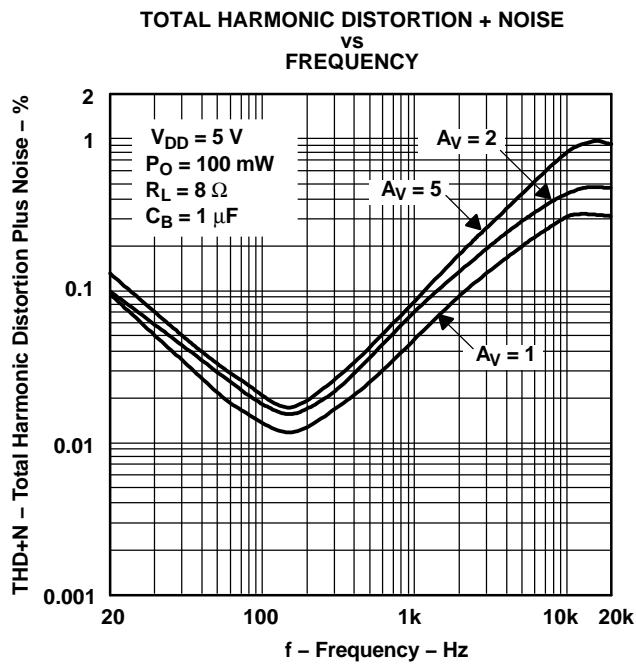


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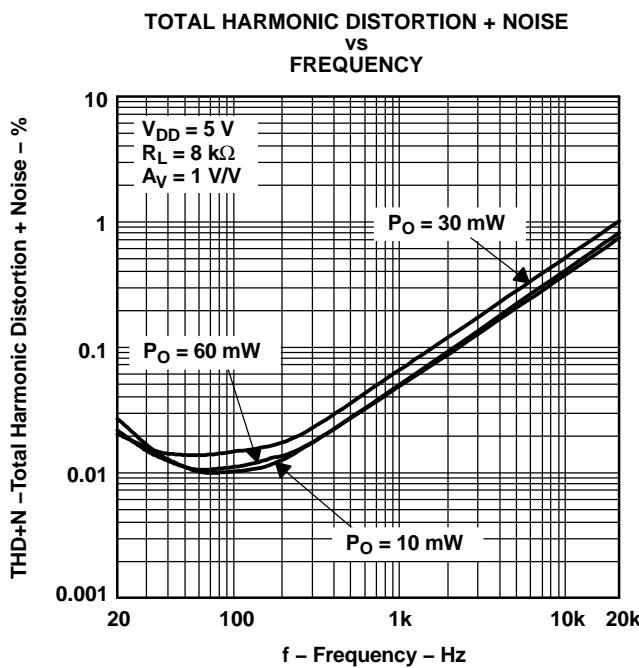


Figure 17.

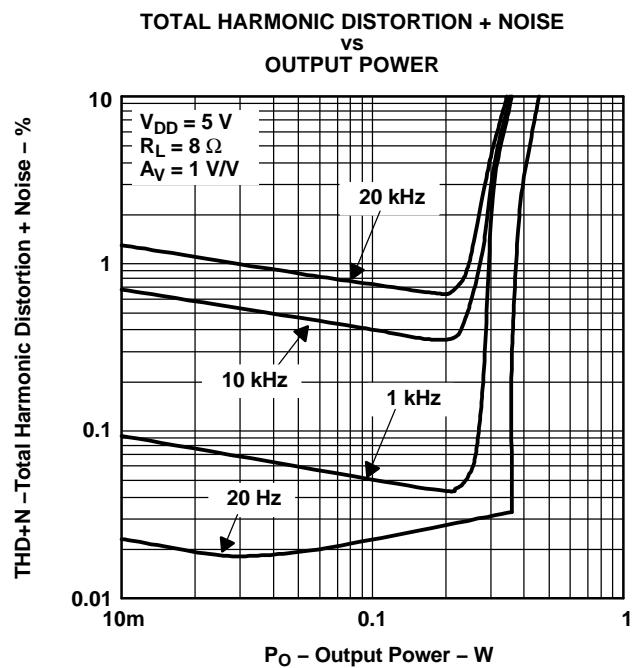


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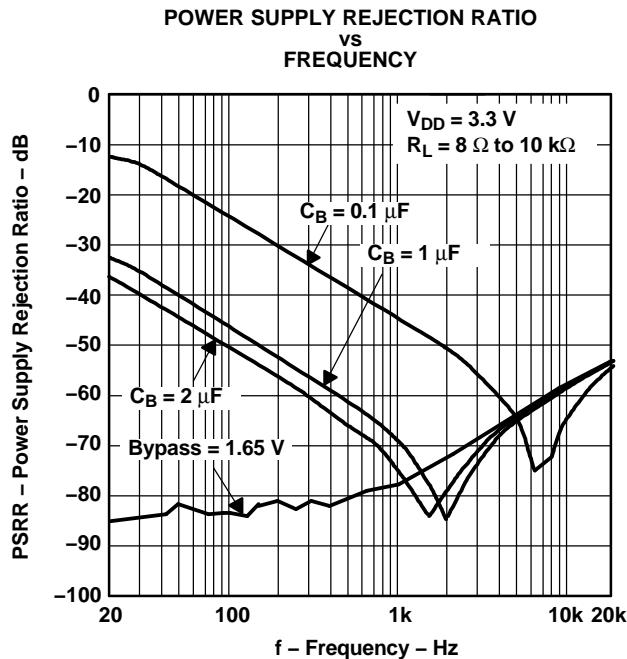


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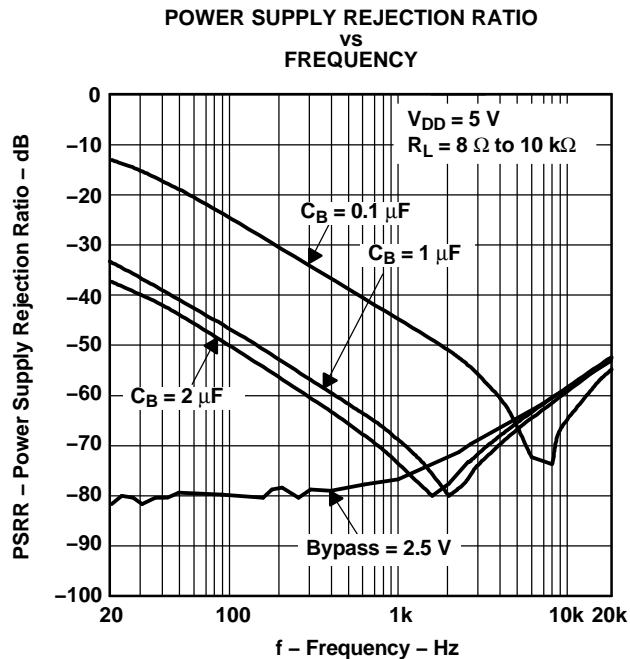


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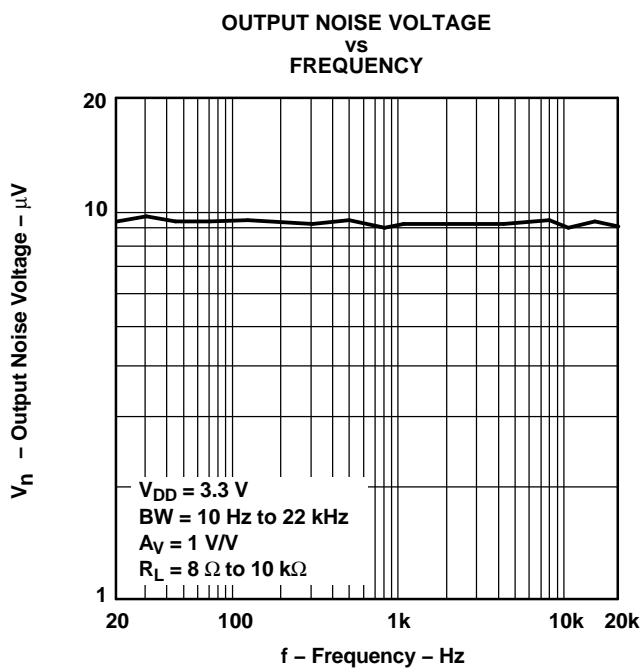


Figure 21.

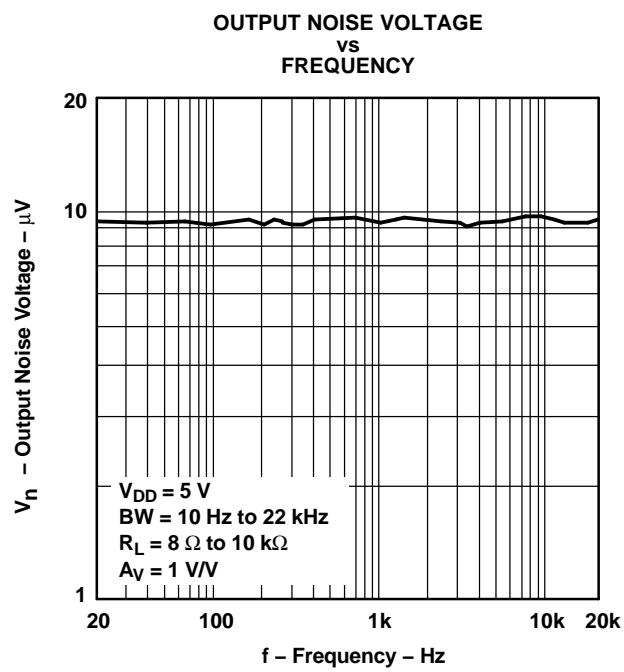


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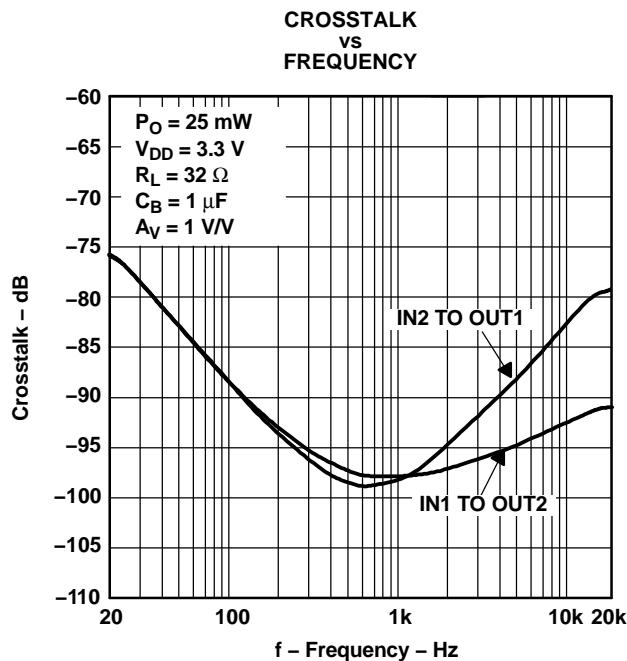


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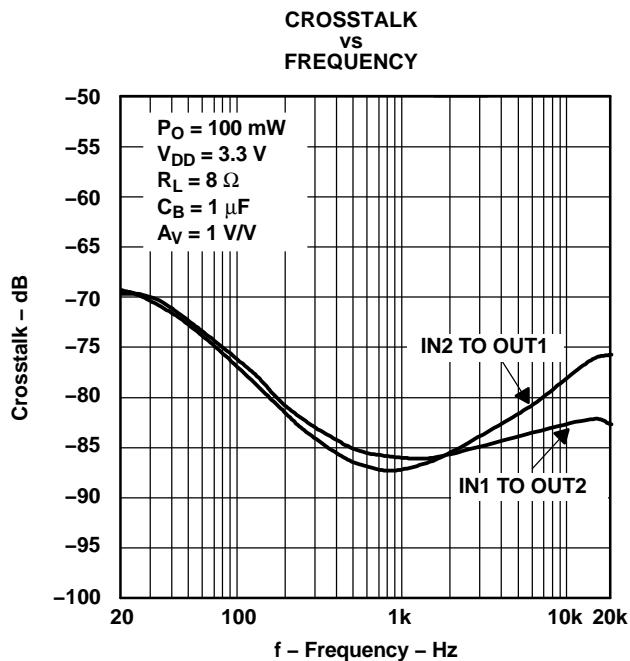


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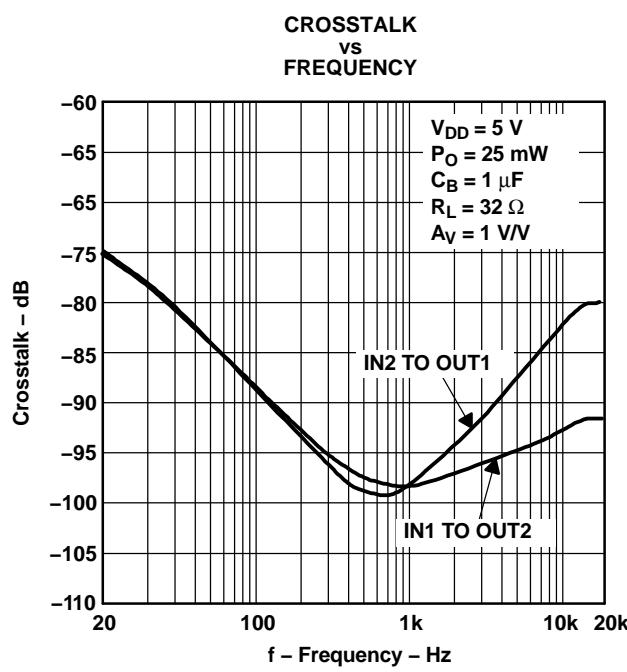


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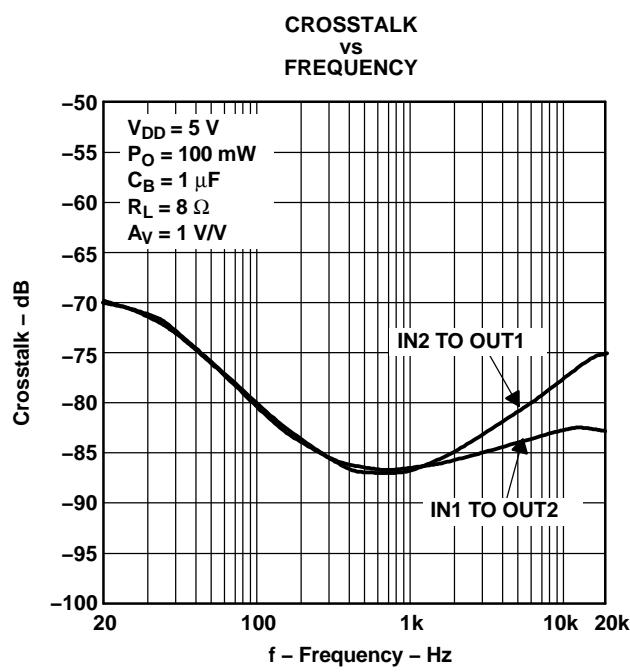


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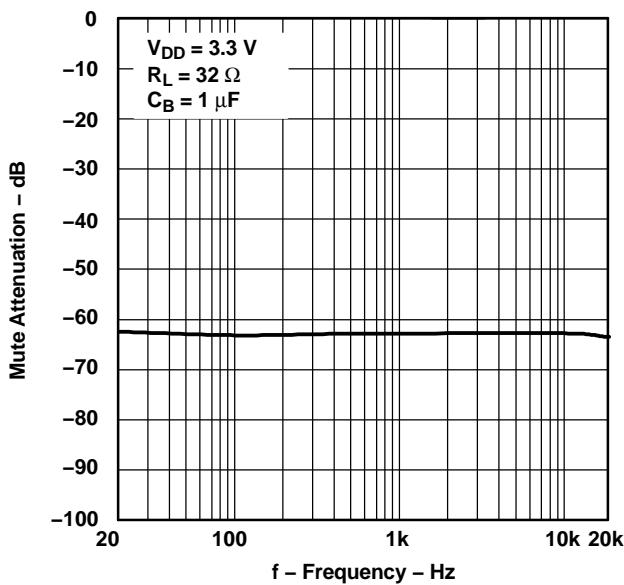
**MUTE ATTENUATION
vs
FREQUENCY**


Figure 27.

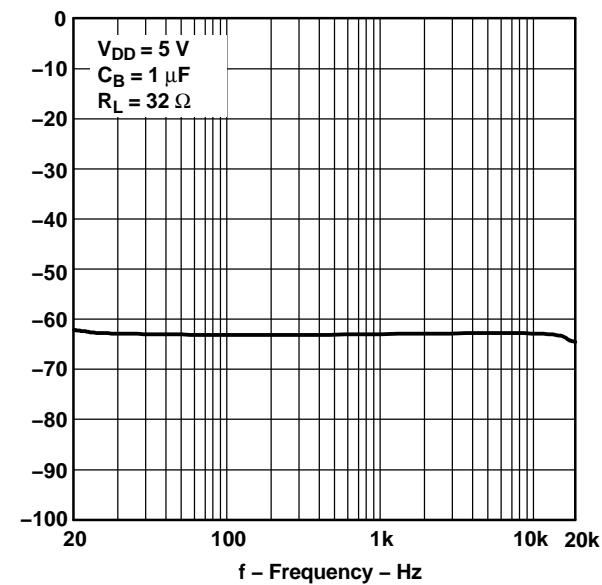
**MUTE ATTENUATION
vs
FREQUENCY**


Figure 28.

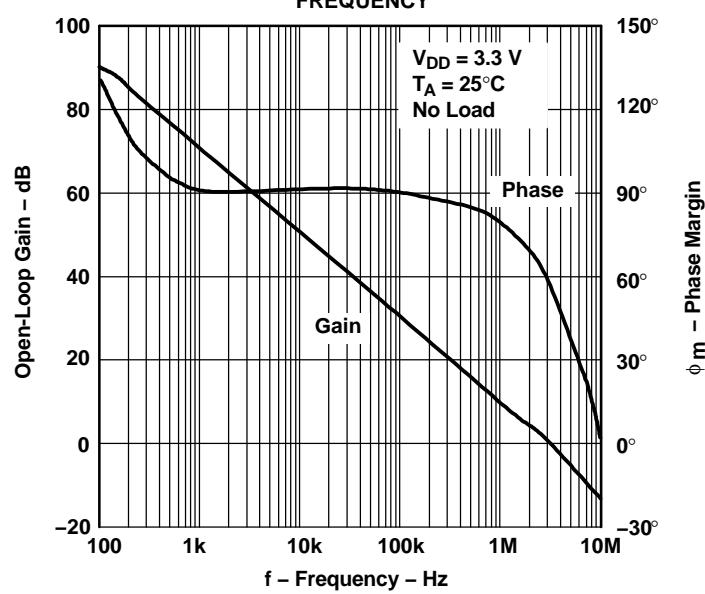
**OPEN-LOOP GAIN AND PHASE MARGIN
vs
FREQUENCY**


Figure 29.

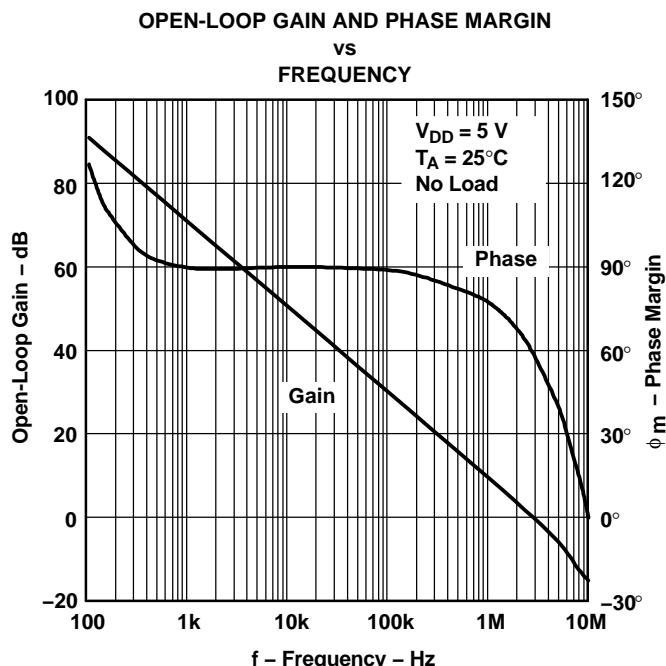


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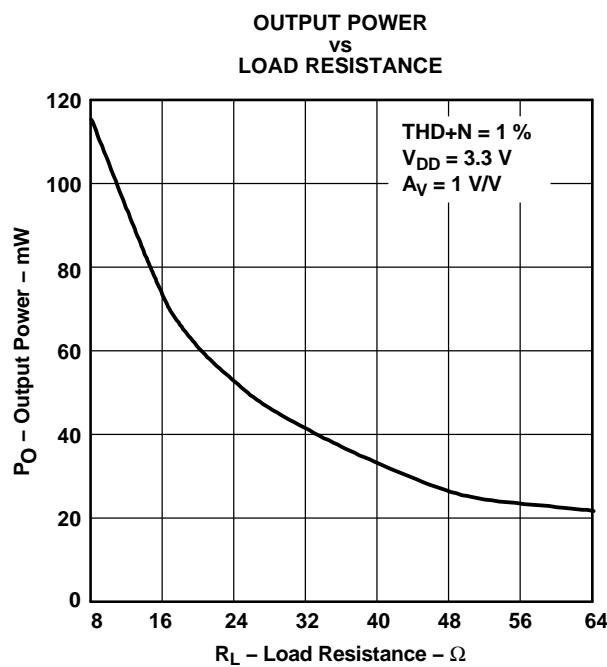


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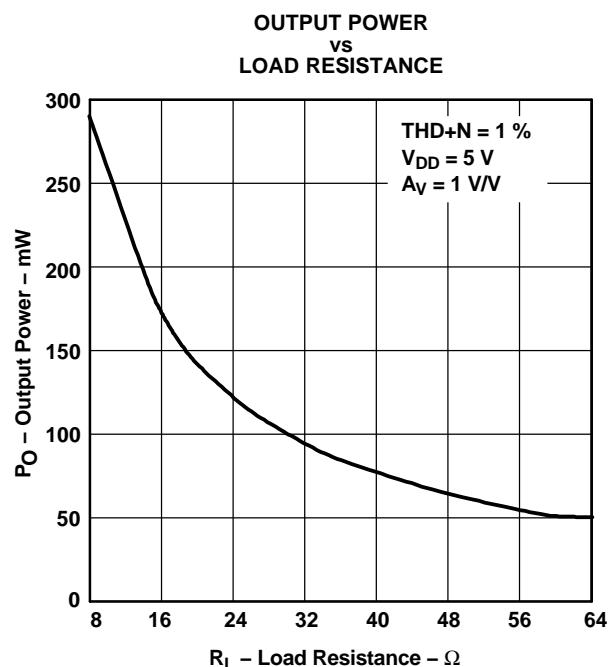


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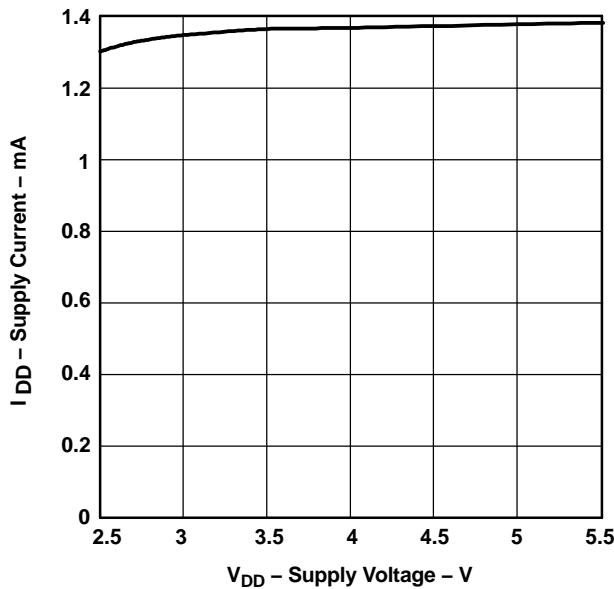
**SUPPLY CURRENT
vs
SUPPLY VOLTAGE**


Figure 33.

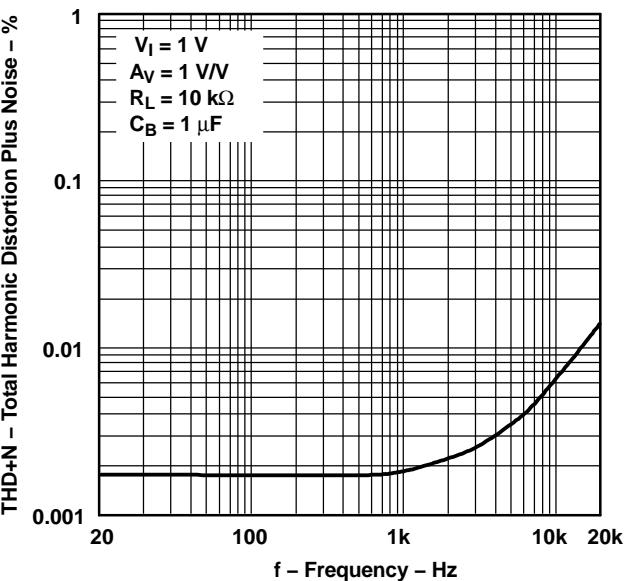
**TOTAL HARMONIC DISTORTION + NOISE
vs
FREQUENCY**


Figure 34.

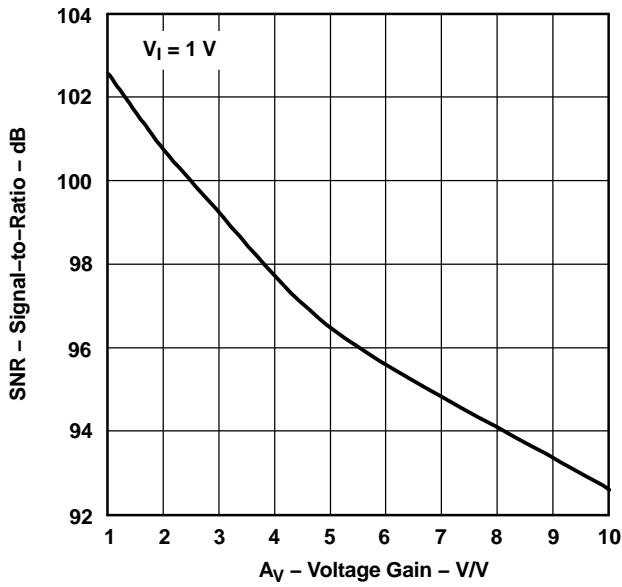
**SIGNAL-TO-NOISE RATIO
vs
VOLTAGE GAIN**


Figure 35.

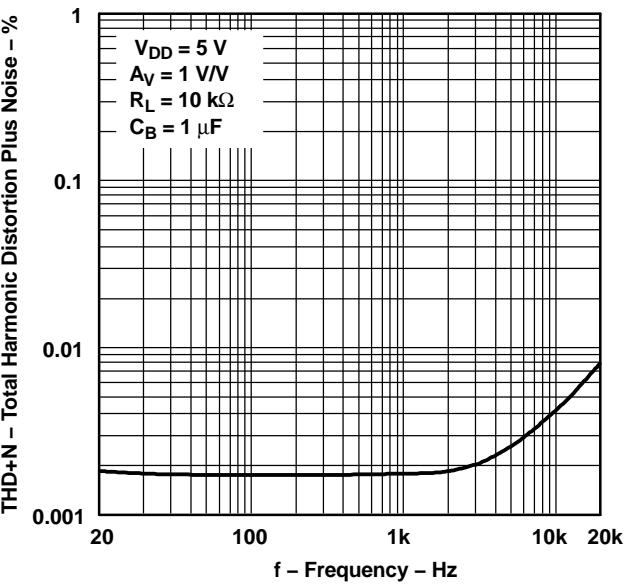
**TOTAL HARMONIC DISTORTION + NOISE
vs
FREQUENCY**


Figure 36.

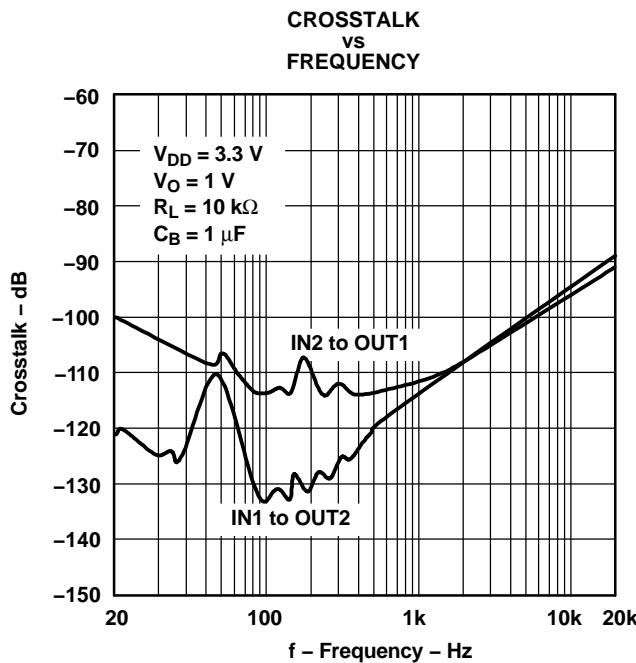


Figure 37.

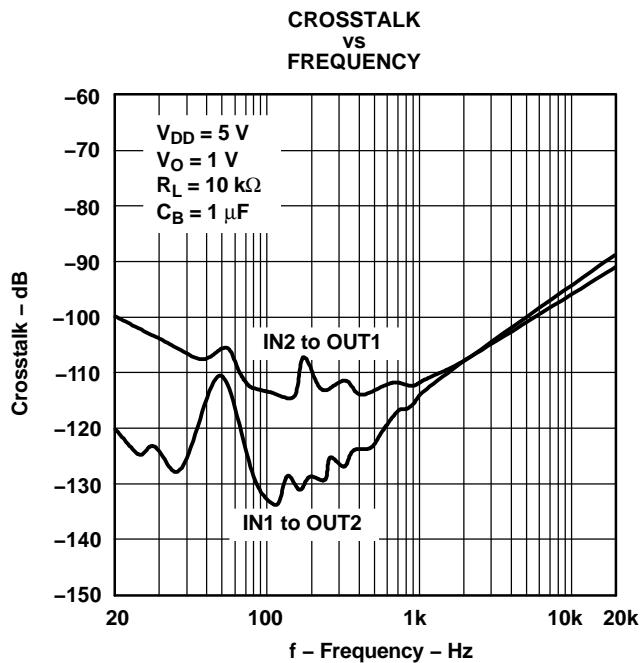


Figure 38.

**CLOSED-LOOP GAIN AND PHASE
vs
FREQUENCY**

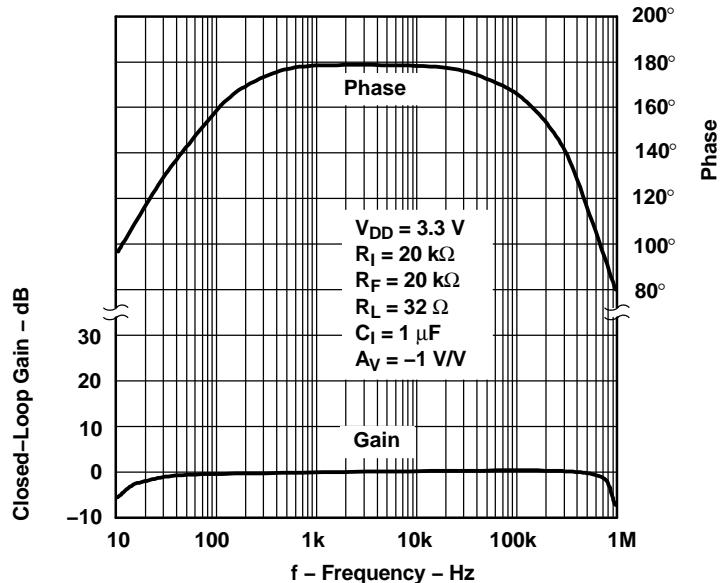


Figure 39.

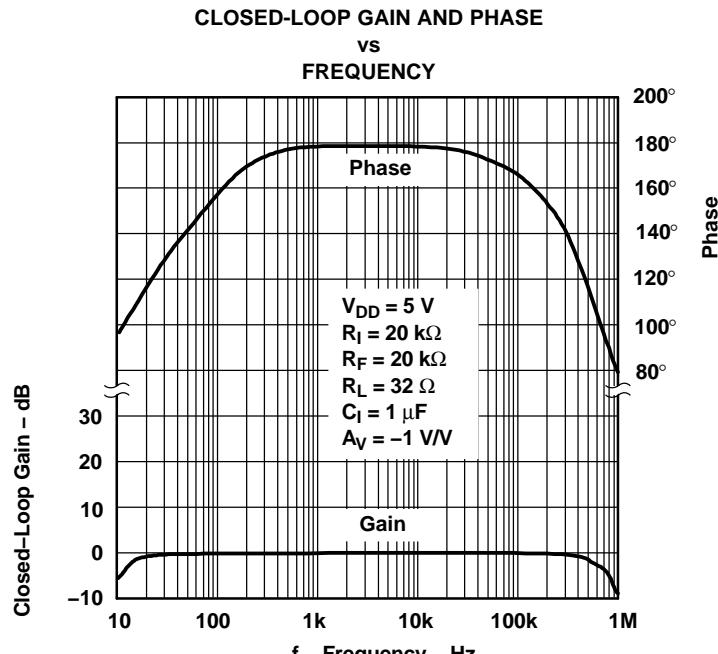


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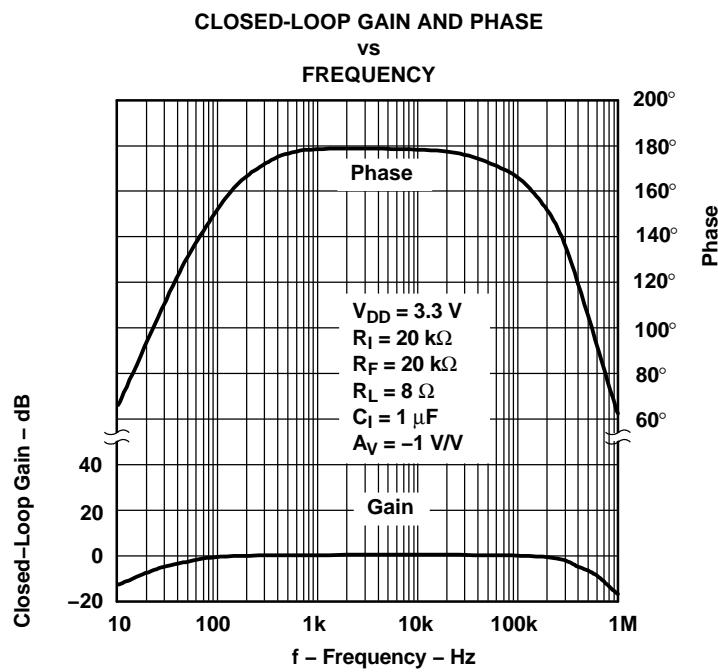


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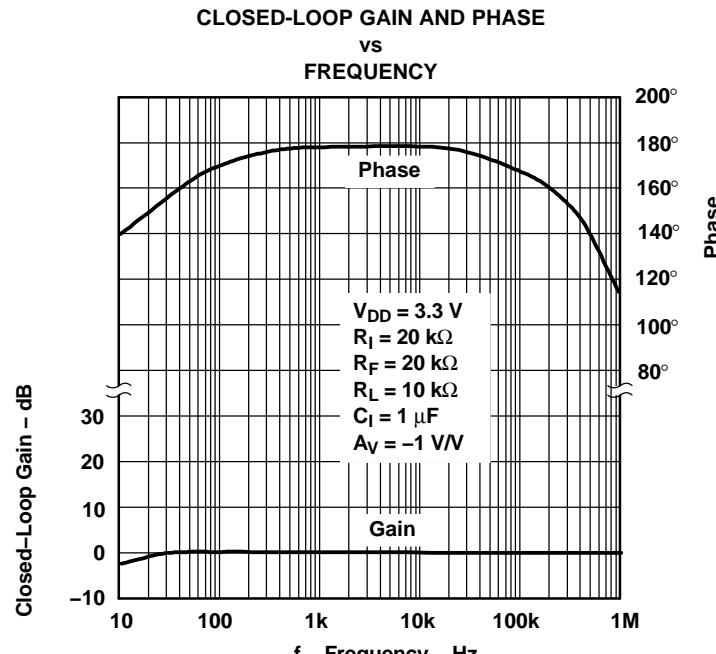


Figure 42.

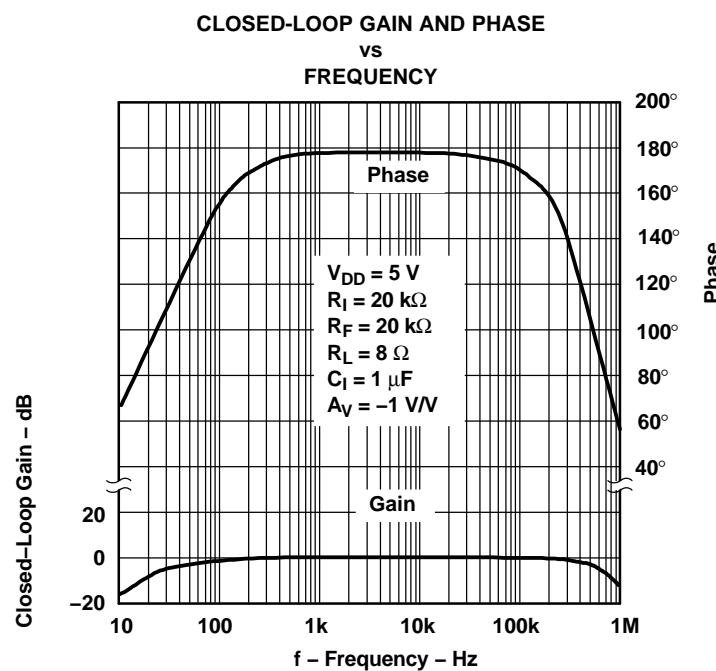


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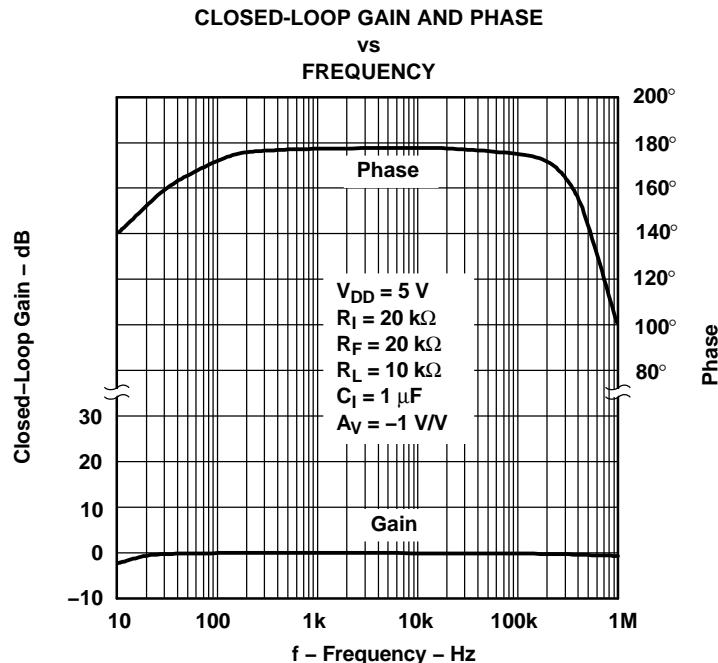


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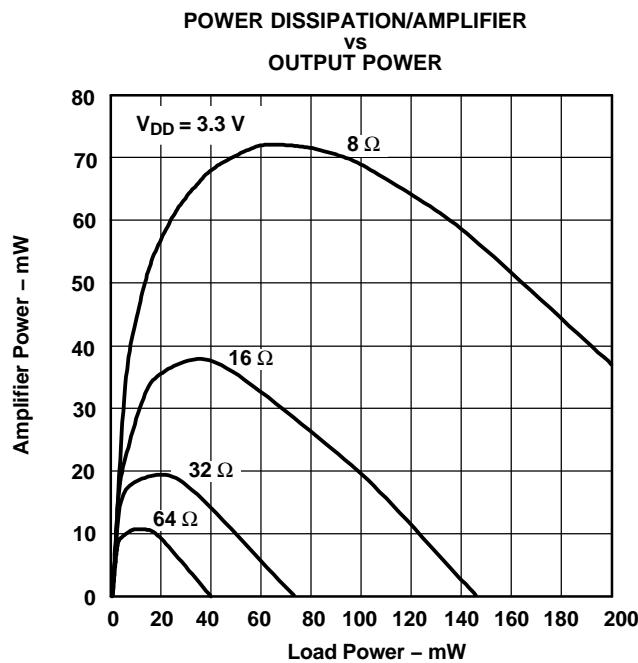


Figure 45.

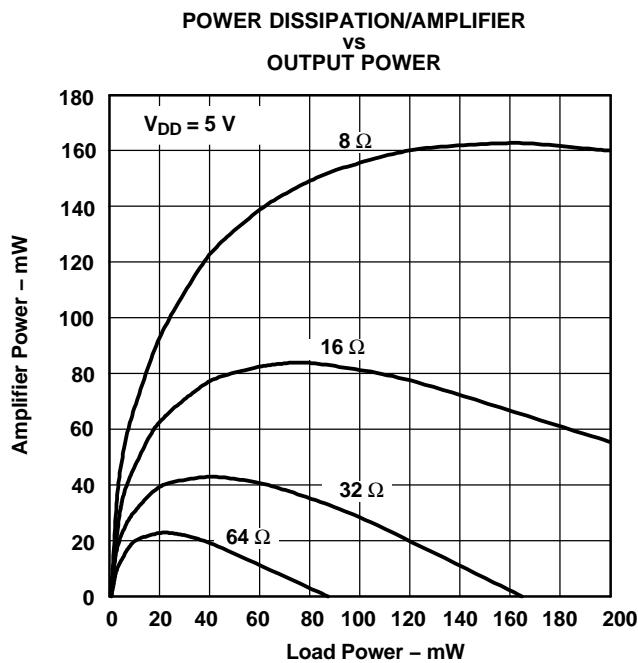


Figure 46.

APPLICATION INFORMATION

GAIN SETTING RESISTORS, R_F and R_I

The gain for the TPA112 is set by resistors R_F and R_I according to Equation 1.

$$\text{Gain} = -\left(\frac{R_F}{R_I}\right) \quad (1)$$

Given that the TPA112 is an MOS amplifier, the input impedance is high. Consequently, input leakage currents are not generally a concern, although noise in the circuit increases as the value of R_F increases. In addition, a certain range of R_F values is required for proper start-up operation of the amplifier. Taken together, it is recommended that the effective impedance seen by the inverting node of the amplifier be set between 5 k Ω and 20 k Ω . The effective impedance is calculated in Equation 2.

$$\text{Effective Impedance} = \frac{R_F R_I}{R_F + R_I} \quad (2)$$

As an example, consider an input resistance of 20 k Ω and a feedback resistor of 20 k Ω . The gain of the amplifier would be -1 and the effective impedance at the inverting terminal would be 10 k Ω , which is within the recommended range.

For high-performance applications, metal film resistors are recommended because they tend to have lower noise levels than carbon resistors. For values of R_F above 50 k Ω , the amplifier tends to become unstable due to a pole formed from R_F and the inherent input capacitance of the MOS input structure. For this reason, a small compensation capacitor of approximately 5 pF should be placed in parallel with R_F . In effect, this creates a low-pass filter network with the cutoff frequency defined in Equation 3.

$$f_{\text{co(lowpass)}} = \frac{1}{2\pi R_F C_F} \quad (3)$$

For example, if R_F is 100 k Ω and C_F is 5 pF then $f_{\text{co(lowpass)}}$ is 318 kHz, which is well outside the audio range.

INPUT CAPACITOR, C_I

In the typical application, input capacitor C_I is required to allow the amplifier to bias the input signal to the proper dc level for optimum operation. In this case, C_I and R_I form a high-pass filter with the corner frequency determined in Equation 4.

$$f_{\text{co(highpass)}} = \frac{1}{2\pi R_I C_I} \quad (4)$$

The value of C_I is important to consider, as it directly affects the bass (low-frequency) performance of the circuit. Consider the example where R_I is 20 k Ω and the specification calls for a flat bass response down to 20 Hz. Equation 4 is reconfigured as Equation 5.

$$C_I = \frac{1}{2\pi R_I f_{\text{co(highpass)}}} \quad (5)$$

In this example, C_I is 0.4 μ F, so one would likely choose a value in the range of 0.47 μ F to 1 μ F. A further consideration for this capacitor is the leakage path from the input source through the input network (R_I , C_I) and the feedback resistor (R_F) to the load. This leakage current creates a dc offset voltage at the input to the amplifier that reduces useful headroom, especially in high-gain applications (> 10). For this reason a low-leakage tantalum or ceramic capacitor is the best choice. When polarized capacitors are used, the positive side of the capacitor should face the amplifier input in most applications, as the dc level there is held at $V_{DD}/2$, which is likely higher than the source dc level. It is important to confirm the capacitor polarity in the application.

APPLICATION INFORMATION (continued)

POWER SUPPLY DECOUPLING, C_s

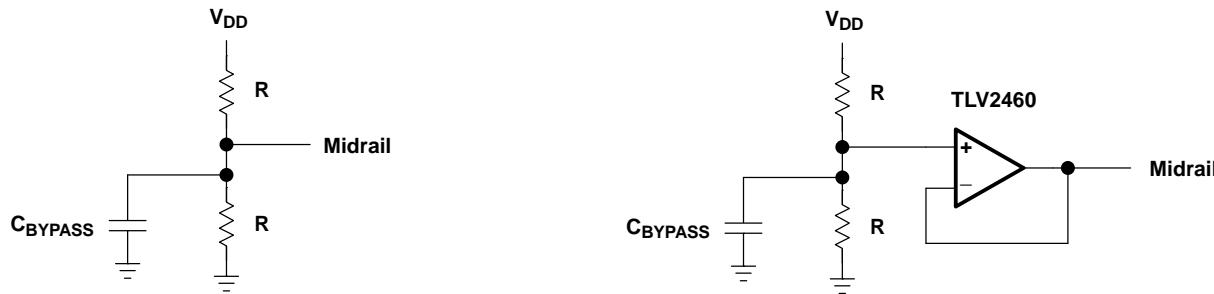
The TPA112 is a high-performance CMOS audio amplifier that requires adequate power supply decoupling to ensure that the output total harmonic distortion (THD) is as low as possible. Power supply decoupling also prevents oscillations for long lead lengths between the amplifier and the speaker. The optimum decoupling is achieved by using two capacitors of different types that target different types of noise on the power supply leads. For higher frequency transients, spikes, or digital hash on the line, a good low equivalent-series-resistance (ESR) ceramic capacitor; typically, 0.1 μ F, placed as close as possible to the device V_{DD} lead, works best. For filtering lower frequency noise signals, a larger aluminum electrolytic capacitor of 10 μ F or greater placed near the power amplifier is recommended.

MIDRAIL VOLTAGE

The TPA112 is a single-supply amplifier; so, it must be properly biased to accommodate audio signals. Normally, the amplifier is biased at $V_{DD}/2$, but it can actually be biased at any voltage between V_{DD} and ground. However, biasing the amplifier at a point other than $V_{DD}/2$ reduces the amplifier's maximum output swing. In some applications where the circuitry driving the TPA112 has a different midrail voltage, it might make sense to use the same midrail voltage for the TPA112, and possibly eliminate the use of the dc-blocking capacitors.

The two concerns with the midrail voltage source are the amount of noise present and its output impedance. Any noise present on the midrail voltage source that is not present on the audio input signal will be input to the amplifier, and passed to the output (and increased by the gain of the circuit). Common-mode noise is cancelled out by the differential configuration of the circuit.

The output impedance of the circuit used to generate the midrail voltage needs to be low enough so as not to be influenced by the audio signal path. A common method of generating the midrail voltage is to form a voltage divider from the supply to ground, with a bypass capacitor from the common node to ground. This capacitor improves the PSRR of the circuit. However, this circuit has a limited range of output impedances; so, to achieve low output impedances, the voltage generated by the voltage divider is fed into a unity-gain amplifier to lower the output impedance of the circuit.



a) Midrail Voltage Generator Using a Simple Resistor-Divider

b) Buffered Midrail Voltage Generator to Provide Low Output Impedance

Figure 47. Midrail Voltage Generator

If a voltage step is applied to a speaker, it causes a noise pop. To reduce popping, the midrail voltage should rise at a subsonic rate. That is, a rate less than the rise time of a 20-Hz waveform. If the voltage rises faster than that, there is the possibility of a pop from the speaker.

Pop can also be heard in the speaker if the midrail voltage rises faster than the charge of either the input coupling capacitor or the output coupling capacitor. If midrail rises first, the charging of the input and output capacitors is heard in the speaker. To keep this noise as low as possible, the relationship shown in Equation 6 should be maintained.

APPLICATION INFORMATION (continued)

$$\frac{1}{(C_B \times R_{\text{SOURCE}})} \leq \frac{1}{(C_I R_I)} \ll \frac{1}{R_L C_C} \quad (6)$$

Where C_{BYPASS} is the value of the bypass capacitor, and R_{SOURCE} is the equivalent source impedance of the voltage divider (the parallel combination of the two resistors). For example, if the voltage divider is constructed using two 20-k Ω resistors, then R_{SOURCE} is 10 k Ω .

MIDRAIL BYPASS CAPACITOR, C_B

The midrail bypass capacitor C_B serves several important functions. During start-up, C_B determines the rate at which the amplifier starts up. This helps to push the start-up pop noise into the subaudible range (so slow it can not be heard). The second function is to reduce noise produced by the power supply caused by coupling into the output drive signal. This noise is from the midrail generation circuit internal to the amplifier. The capacitor is fed from the resistor divider with equivalent resistance of R_{SOURCE} . To keep the start-up pop as low as possible, the relationship shown in Equation 7 should be maintained.

$$\frac{1}{(C_B \times R_{\text{SOURCE}})} \leq \frac{1}{(C_I R_I)} \quad (7)$$

As an example, consider a circuit where C_B is 1 μF , $R_{\text{SOURCE}} = 160 \text{ k}\Omega$, C_I is 1 μF , and R_I is 20 k Ω . Inserting these values into the Equation 8 results in:

$$6.25 \leq 50 \quad (8)$$

which satisfies the rule. Recommended values for bypass capacitor C_B are 0.1 μF to 1 μF , ceramic or tantalum low-ESR, for the best THD and noise performance.

OUTPUT COUPLING CAPACITOR, C_C

In the typical single-supply, single-ended (SE) configuration, an output coupling capacitor (C_C) is required to block the dc bias at the output of the amplifier, thus preventing dc currents in the load. As with the input coupling capacitor, the output coupling capacitor and impedance of the load form a high-pass filter governed by Equation 9.

$$f_{(\text{out high})} = \frac{1}{2\pi R_L C_C} \quad (9)$$

The main disadvantage, from a performance standpoint, is that the typically small load impedances drive the low-frequency corner higher. Large values of C_C are required to pass low frequencies into the load. Consider the example where a C_C of 68 μF is chosen and loads vary from 32 Ω to 47 k Ω . Table 1 summarizes the frequency response characteristics of each configuration.

Table 1. Common Load Impedances vs Low Frequency Output Characteristics in SE Mode

R_L	C_C	LOWEST FREQUENCY
32 Ω	68 μF	73 Hz
10,000 Ω	68 μF	0.23 Hz
47,000 Ω	68 μF	0.05 Hz

As Table 1 indicates, headphone response is adequate and drive into line level inputs (a home stereo for example) is good.

The output coupling capacitor required in single-supply, SE mode also places additional constraints on the selection of other components in the amplifier circuit. With the rules described earlier still valid, add the following relationship:

- **Output Pulldown Resistor, $R_C + R_O$**

– Placing a 100- Ω resistor, R_C , from the output side of the coupling capacitor to ground ensures the coupling capacitor, C_C , is charged before a plug is inserted into the jack. Without this resistor, the coupling capacitor would charge rapidly upon insertion of a plug, leading to an audible pop in the headphones.

– Placing a 20-k Ω resistor, R_O , from the output of the IC to ground ensures that the coupling capacitor fully discharges at power down. If the supply is rapidly cycled without this capacitor, a small pop may be audible in 10-k Ω loads.

- **Using Low-ESR Capacitors**

– Low-ESR capacitors are recommended throughout this application. A real capacitor can be modeled simply as a resistor in series with an ideal capacitor. The voltage drop across this resistor minimizes the beneficial effects of the capacitor in the circuit. The lower the equivalent value of this resistance, the more the real capacitor behaves like an ideal capacitor.

5-V VERSUS 3.3-V OPERATION

The TPA112 is designed for operation over a supply range of 2.5 V to 5.5 V. This data sheet provides full specifications for 5-V and 3.3-V operation because these are considered to be the two most common standard voltages. There are no special considerations for 3.3-V versus 5-V operation as far as supply bypassing, gain setting, or stability. The most important consideration is that of output power. Each amplifier in the TPA112 can produce a maximum voltage swing of $V_{DD} - 1$ V. This means, for 3.3-V operation, clipping starts to occur when $V_{O(PP)} = 2.3$ V, as opposed to $V_{O(PP)} = 4$ V for 5-V operation. The reduced voltage swing subsequently reduces maximum output power into the load before distortion begins to become significant.

PACKAGING INFORMATION

Orderable part number	Status (1)	Material type (2)	Package Pins	Package qty Carrier	RoHS (3)	Lead finish/ Ball material (4)	MSL rating/ Peak reflow (5)	Op temp (°C)	Part marking (6)
TPA112D	Obsolete	Production	SOIC (D) 8	-	-	Call TI	Call TI	-	
TPA112DR	Active	Production	SOIC (D) 8	2500 LARGE T&R	Yes	NIPDAU	Level-1-260C-UNLIM	-	TPA112
TPA112DR.A	Active	Production	SOIC (D) 8	2500 LARGE T&R	Yes	NIPDAU	Level-1-260C-UNLIM	See TPA112DR	TPA112

⁽¹⁾ **Status:** For more details on status, see our [product life cycle](#).

⁽²⁾ **Material type:** When designated, preproduction parts are prototypes/experimental devices, and are not yet approved or released for full production. Testing and final process, including without limitation quality assurance, reliability performance testing, and/or process qualification, may not yet be complete, and this item is subject to further changes or possible discontinuation. If available for ordering, purchases will be subject to an additional waiver at checkout, and are intended for early internal evaluation purposes only. These items are sold without warranties of any kind.

⁽³⁾ **RoHS values:** Yes, No, RoHS Exempt. See the [TI RoHS Statement](#) for additional information and value definition.

⁽⁴⁾ **Lead finish/Ball material:** Parts may have multiple material finish options. Finish options are separated by a vertical ruled line. Lead finish/Ball material values may wrap to two lines if the finish value exceeds the maximum column width.

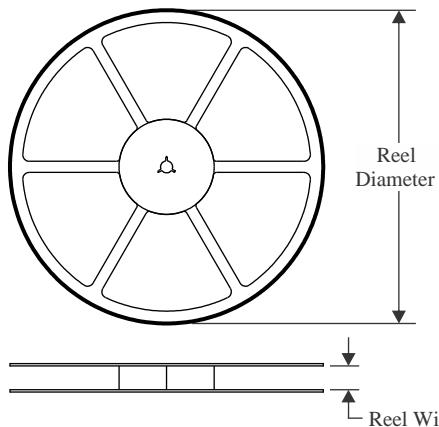
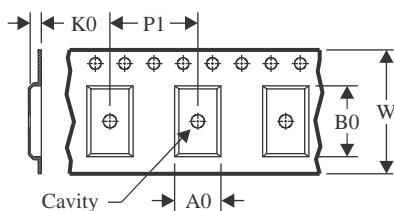
⁽⁵⁾ **MSL rating/Peak reflow:** The moisture sensitivity level ratings and peak solder (reflow) temperatures. In the event that a part has multiple moisture sensitivity ratings, only the lowest level per JEDEC standards is shown. Refer to the shipping label for the actual reflow temperature that will be used to mount the part to the printed circuit board.

⁽⁶⁾ **Part marking:** There may be an additional marking, which relates to the logo, the lot trace code information, or the environmental category of the part.

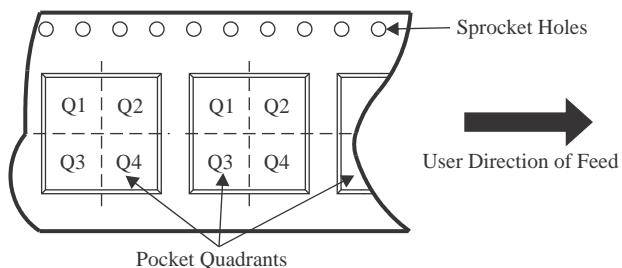
Multiple part markings will be inside parentheses. Only one part marking contained in parentheses and separated by a "~" will appear on a part. If a line is indented then it is a continuation of the previous line and the two combined represent the entire part marking for that device.

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TAPE AND REEL INFORMATION
REEL DIMENSIONS

TAPE DIMENSIONS


A0	Dimension designed to accommodate the component width
B0	Dimension designed to accommodate the component length
K0	Dimension designed to accommodate the component thickness
W	Overall width of the carrier tape
P1	Pitch between successive cavity centers

QUADRANT ASSIGNMENTS FOR PIN 1 ORIENTATION IN TAPE


*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Reel Diameter (mm)	Reel Width W1 (mm)	A0 (mm)	B0 (mm)	K0 (mm)	P1 (mm)	W (mm)	Pin1 Quadrant
TPA112DR	SOIC	D	8	2500	330.0	12.4	6.4	5.2	2.1	8.0	12.0	Q1

TAPE AND REEL BOX DIMENSIONS


*All dimensions are nominal

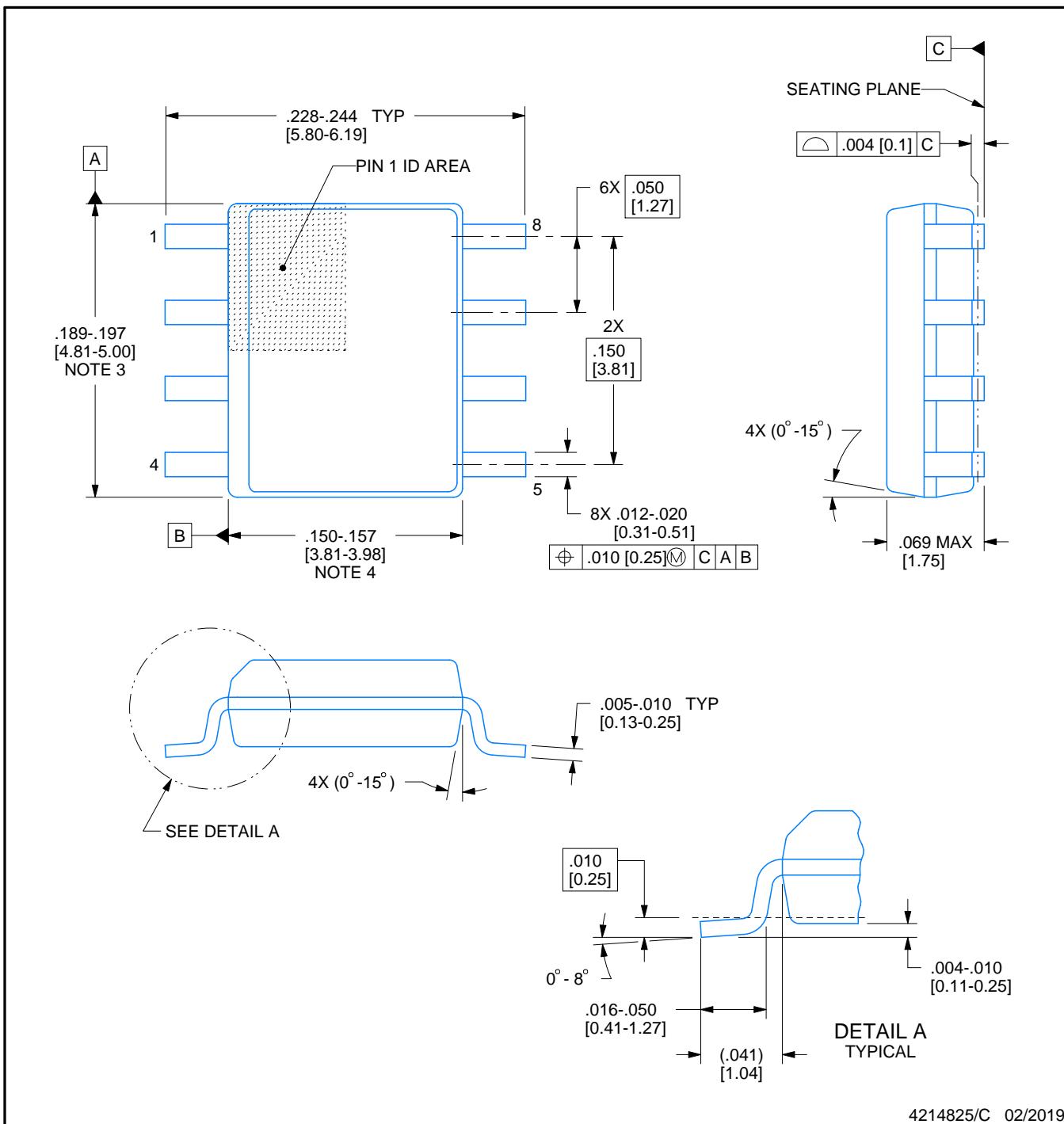
Device	Package Type	Package Drawing	Pins	SPQ	Length (mm)	Width (mm)	Height (mm)
TPA112DR	SOIC	D	8	2500	350.0	350.0	43.0



PACKAGE OUTLINE

SOIC - 1.75 mm max height

SMALL OUTLINE INTEGRATED CIRCUIT



NOTES:

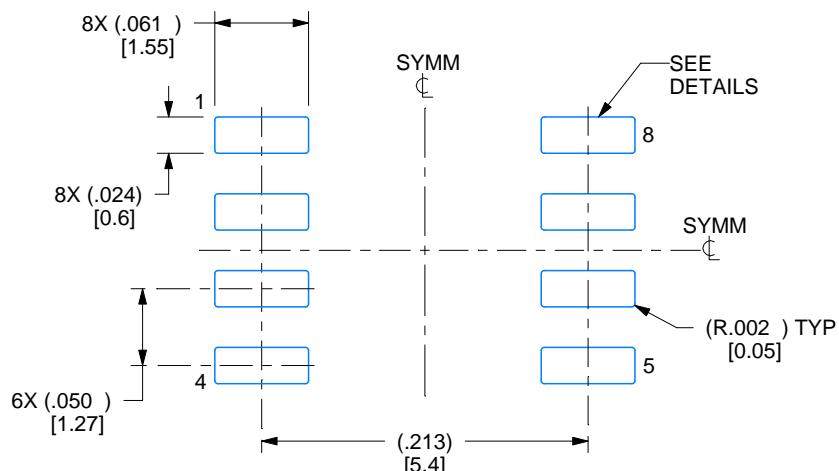
1. Linear dimensions are in inches [millimeters]. Dimensions in parenthesis are for reference only. Controlling dimensions are in inches. Dimensioning and tolerancing per ASME Y14.5M.
2. This drawing is subject to change without notice.
3. This dimension does not include mold flash, protrusions, or gate burrs. Mold flash, protrusions, or gate burrs shall not exceed .006 [0.15] per side.
4. This dimension does not include interlead flash.
5. Reference JEDEC registration MS-012, variation AA.

EXAMPLE BOARD LAYOUT

D0008A

SOIC - 1.75 mm max height

SMALL OUTLINE INTEGRATED CIRCUIT



LAND PATTERN EXAMPLE
EXPOSED METAL SHOWN
SCALE:8X



SOLDER MASK DETAILS

4214825/C 02/2019

NOTES: (continued)

6. Publication IPC-7351 may have alternate designs.

7. Solder mask tolerances between and around signal pads can vary based on board fabrication site.

EXAMPLE STENCIL DESIGN

D0008A

SOIC - 1.75 mm max height

SMALL OUTLINE INTEGRATED CIRCUIT



SOLDER PASTE EXAMPLE
BASED ON .005 INCH [0.125 MM] THICK STENCIL
SCALE:8X

4214825/C 02/2019

NOTES: (continued)

8. Laser cutting apertures with trapezoidal walls and rounded corners may offer better paste release. IPC-7525 may have alternate design recommendations.
9. Board assembly site may have different recommendations for stencil design.

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